

engineering principles and practices

August 1995

New Power FETS Offer Low Cost in Standard Packages

Featured Technology — Designing with RFICs

Tutorial IMD Measurements



Wireless International Corp. solves tough test problems.

As test engineers and designers, you understand the importance of efficient and effective testing for development and production testing. Poor test methods and inaccurate measurements can bring the production of the best designed equipment to a crawl. Wireless International Corp. (WIC) has answered these problems with plug-in-and-run test systems which provide stimulus, control, and measurement capabilities at your fingertips. Here are just a few of the test solutions.



CDMA Multipath and AWGN test station.

For CDMA testing, WIC's MP-CDMA test system generates multipath and additive noise as specified by IS-98. This system is comprised of the multipath emulator, a precision carrier-to-noise generator, an integrated 486DX/33 computer, and control software with a graphics user interface. The precision carrier-to-noise generator has been designed specifically to operate with extreme accuracy even under the difficult conditions of slow fading for which CDMA systems must be tested. Available frequency ranges are between 800 and 2500 MHz.

INFO/CARD 1

INFO/CARD 04

With its new integrated test system, Wireless International Corp. steps to the head of the class.

Multichannel Eb/No versus BER test station.

A R O A R D A R D A R D A R D A R D A R D A R D A R D A R D A R D A R D A R D A R D A R D A R D A R D A R D A R

If you are performing BER versus Eb/No curves for multiple devices simultaneously, then here is your test equipment answer. WIC's Series 800 test stations can generate these curves for up to 8 channels simultaneously, all under the control of a single integrated computer or via the IEEE-488 interface. Each channel contains a precision carrier-to-noise generator and a programmable bit error rate tester. Bit errors and bit error rate data are stored to disk for analysis. Eb/No versus BER curves are generated in both tabular and graphical form for hard-copy output. Data rates up to 8 X 10 MBPS are programmable with error insertion rate, bit slip, and PN code length selections.

A look into the future.

WIC's products are modular to provide easy upgrading. So the instrument that you buy today won't be obsolete tomorrow.

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SPECIFICATION	s			Midban	d (dB,	Typ.)	
	LO	Freq.	(MHz)	Conv.	Is	ol.	\$ea.
Model	(dBm)	LO/RF	IF	Loss	L-R	L-I	(qty. 1-9)
JMS-1	+7	2-500	DC-500	5.75	45	45	4.95
JMS-1LH	+10	2-500	DC-500	5.75	55	45	8.45
JMS-1MH	+13	2-500	DC-500	5.75	60	45	9.45
JMS-1H	+17	2-500	DC-500	5.90	50	50	11.45
JMS-2L	+3	800-1000	DC-200	7.0	24	20	7.45
JMS-2	+7	20-1000	DC-1000	7.0	50	47	7.45
JMS-2LH	+10	20-1000	DC-1000	6.5	48	35	9.45
JMS-2MH	+13	20-1000	DC-1000	7.0	50	47	10.45
JMS-2H	+17	2 0-1 000	DC-1000	7.0	50	47	12.45
JMS-2W	+7	5-1200	DC-500	6.8	60	48	7.95
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Note: *10-49 qty.



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- 10

88

1765

776

FREQ

(MF33)

1.35 137

34 20 60

104

868



.

MODEL MGA-10D MOA:3HD MICA 200 MOC-WO

MOV 1.250 MOV 700 MOV 1400

ICIO-RO/D

JOC-170

I/Q MO	DULATOR	RS		
CONV. LOSS	CAPHER REJ	SCEBA D REJ	HAPM	PRICE
× 0	(-dBc) Typ.	(-altic) Typ_	(-080) Iyp. 34/0 55/0	(1+9)
58 0.20	2 41 50	-40 40	58 68 48 65	49-96
62 0.10	38	38 30	48 58	39.95
55 010	1 38	38	48 58	48.95
55 0.10	38	-36 38	40 50 40 56	49.95 411.95
16.0.10	48	.07	54 65	40.95
55 010	38	36	47 70	54.95
90 0.30	35	35	8 65 65 40 45	09.05
5.8 020 5.8 020	40	35 36	47 60 45 60	19.95
Surface	Mount Mod	Ande		
58.01	40	32	45 00	49.95

1/O DEMODUL ATORS

8 02 02

OL IX	CNN OSS VB) O	AMP. UNBAL IOEE Typ.	PHASE UNEAL (Dig.) Typ.	HAI SLIPF (dB0 3NO	RESS 1 Typ. 54/C	PRIC \$ Ofy (1-9
6.0 6.1 6.2	0.10 0.15 0.10	0.15 0.15 0.15	10 07 07	60 64 50	65 67 68	40.9 49.9 49.9
55 53 8.0	0.10 0.10 0.20	0.10	0.5 1.0 1.5	60 55 40	65 07 50	40.00 70.00 00.90
50	0.10 0.25 0.25	0.15 0.10 0.10	1.0 0.5 0.5	59 52 47	87 68 70	29.00 19.00 19.00
Sur	face Mic	unt Mode	sis			
86	0.1	0.10		45	13.8	54.9 98.9

CQ 18 D 1805 1880 NON-HERMETICALLY SEALED

MIQA case .4 x .8 x .4 in. MIQC case .8 x .8 x .4 in. MIQY case .8 x .8 x .4 in JCIQ case .9 x .8 x .25 in

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50 85



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FO/CARD 3

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40 Low Dropout Current Source Protects Silicon MMICs and Transistors

Voltage dropout circuit sensitivities and excessive power dissiption have made

designing bias circuits which operate near a device's maximum voltage level difficult. This article describes a circuit which provides stable bias with minimal power dissipation. — John V. Bellantoni

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46 Low Cost 1000 Watt, 300 Volt RF Power Amplifier for 13.56 MHz

This article details the design, development, assembly and performance of a 1000 watt, 13.56 MHz RF power amplifier. The amplifier operates from a 300 VDC supply, with an efficiency of 80 percent and uses a "symmetric pair" of low cost RF power MOSFETs from Advanced Power Technology. — Kenneth Dierberger, Bobby McDonald, Lee B. Max

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This article presents the typical tests for intermodulation distortion, an important measure of device linearity and a major factor in receiver performance. — Gary A. Breed

95 Microstrip Coupled-Line Bandpass Filter Synthesis and Analysis Program

A program called BPF.BAS simplifies the task of microstrip coupled line bandpass filter design. The program synthesizes a filter based on desired performance characteristics and provides simple tabular and graphical analyses. — Sean R. Mercer, Ph.D. and Eric Mabada

EMC Pull-Out Section

The August edition of *EMC Test & Design* is included with this issue of *RF Design*. Included is an article about modeling switching power supply emissions, an article about reducing *EMI* of transistors switching inductive loads, and two other articles.



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RF editorial

How Much Do We Need to Know?

By Gary A. Breed Editor

We live in a world where we are completely dependent on technology, yet we have cleverly arranged things so virtually no one understands how that technology works.

> - from an interview with Carl Sagan (paraphrased)

As engineers, it is our job to understand how at least one part of technology works. But, with a clear trend toward integration of technologies in any given product, how much should we know about those other technologies that surround the RF circuitry?

I suppose this is the same question that the medical community faces regarding the value of specialists versus general practitioners. In that field, the trend for several years has been to encourage general practice in order to keep costs under control and promote preventive medicine.

Business has borrowed a term from athletics — cross-training — to describe its efforts to maintain a capable workforce after downsizing has left them with fewer personnel to do the same jobs as before. The secretaries who used to do dictation, typing and filing are now doing sales support or market research. Managers who used to have secretaries now have computers on their desks to do their own letters, memos, and reports.

OK, so what about design engineers? I have always been a proponent of the well-rounded engineer, but that attitude was directed at life *outside* technology; things like the arts, literature, public affairs and sports. I have been forced to re-think my view of the engineer's role in the new inter-disciplinary world. How does an RF engineer



fit into this new scheme where digital, analog, video, power, software and mechanical concerns are addressed simultaneously with RF functionality?

Do we simply maintain our specialty, but with better communications among fellow specialists? Should we try to learn about those other branches of engineering, even if we don't become expert? Or, is it our responsibility to become competent in one or more of these additional specialties? The answer could be any of these.

One point that has become clear is that specialists can no longer be purists — a design team has to balance performance and costs against a product specification. To accomplish a successful design, a minimum level of understanding and acceptance of all aspects of product development goals is necessary. If meeting those goals means learning more about digital design, power circuitry, or manufacturing processes, we must do it.

Remember, low-cost products and rapid development are being re-discovered in the U.S. electronics industry. The engineering profession really is changing; it's not an illusion! To get that next widget into production on time, your company might not find an expert for each part of the design, so someone has to step into that void. You may become the most valuable member of the team by being capable of learning something new. On another product, all the talent necessary may be available, and you need only be a good RF circuit designer with a proper attitude toward teamwork.

"How much do we need to know?" The answer seems to be quite simple: "As much as the job requires."

See You at RF EXPO EAST - August 21-23 - Baltimore, MD

8

ver the last couple of years, we've seen EMC issues evolve from technical "what" questions to regulatory "when" statements. EMC is now, and at Kalmus we're adcressing it head on."

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D. J (Jung

Frank Kalmus Technical Director

Frank Kalmus is the founder of Kalmus (formerly Kalmus Engineering Inc.), a division of Thermo-Voltek Corporation As Kalmus' principal design engineer, he has designed over 200 RF amplifiers used for EMC test, medical/MRL general laboratory, and communications applications.



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Hewlett-Packard specifications are from the HP 437B and HP 438A technical data sheets dated April 1988 and July 1984, respectively.

			_		-
	Capabilities	Giga-tronics 8541	Hewlett- Packard HP 437B	Giga-tronics 8542	Hewlett- Packard HP 438A
	Measurement Speed over GPIB (rdgs/sec)	200	20	200	20
	Measurement Speed using Fast Modes (rdgs/sec)	4,000	Not Available	4,000	Not Available
Compare Your Choices	Maximum Dynamic Range with a Single Sensor	90 dB	50 dB	90 dB	50 dB
	Direct CW and Peak Power Measurements	Yes	No	Yes	No
	Built-in Frequency Cal Factors	Yes	No	Yes	No
	Measurement Channels/Display Lines	One/Two	One/One	Two/Two	Two/One
	Display Pulse Waveform on External Scope	Yes	No	Yes	No
Choose The Alternative	Why Settle F	or The S	Standard	Power	Meter?
					115



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RF letters

Letters should be addressed to: Editor, RF Design, 6300 S. Syracuse Way, Suite 650, Englewood, CO 80111. Letters may be edited for length and clarity.

Another Broadband **Transformer Article** Editor:

It may be of interest to your readers to know that a similar paper [to Don McClure's articles, "Broadband Trarsmission Line Transformer Family Matches a Wide Range of Impedances - Parts 1 & 2, RF Design, Feb. 1994 and May 1995] co-authored by myself and J.D. Harmer was presented and published at the 1974 IEEE International Symposium on Circuits and Systems. The paper is entitled "Transmission Line Transformer with Integer-Ratio Voltage Transformations". If any of your readers are interested, they can contact me for further information or a copy of the paper.

Thomas J. Glusczak 83 Jacobs Rd. Marlboro, MA 01752

[The work on transmission line transformers described in Mr. McClure's article was done well before he wrote his articles for RF Design The patent disclosures for the transformers described in his article are dated April 28, 1972., ed.]

Errata

Tim Dolan, Vice President of Engineering at K&L Microwave was referred to as Tim Nolan in part of July's "Industry Insight" column.

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Upcoming issues will focus on designing for the ISM bands, industrial RF applications, and circuits for DECT & PCS applications. Let other engineers know about your work in these and other areas!

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LIFD-3010-080	30	10	-70 to +5	110	1
LIFD-3010P-80	30	10	-80 to 0	100	0.5
LIFD-6010-70	60	10	-70 to 0	65	1
LIFD-6020P-80	60	20	-80 to 0	50	0.5
LIFD-12020-80	120	20	-80 to 0	50	1
LIFD-16040P-70	160	40	-65 to +5	25	0.5
LIFD-16040-70	160	40	-70 to 0	30	1
LIFD-300100-60	300	100	-60 to 0	10	1

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- Operating frequencies from 250 to 2000 MHz
- Improved sensitivity from 6 dB typical noise figure

Model Number	Center Frequency (MHz)	Bandwidth (3 dB) (MHz, Min.)	Dynamic Range (dB, Min.)	Rise Time (ns, Max.)	Linearity (±dB, Max.)
MLIF-500/100-70	500	100	-70 to 0	10	1
MLIF-750/500-62	750	500	-65 to 0	2	1
MLIF-1000/250-60	1000	250	-60 to 0	2	1
MLIF-1000/500-65	1000	500	-65 to 3	5	1.5
MLIF-1500/1000-60	1500	1000	-60 to 0	1.25	1
MLIF-1575/20-40*	1575	20	-38 to 3	N/A	1.5

* 1.25" x 1" package available for RSSI module used in GPS applications

Frequency Discriminator

- Operating frequencies from 21 to 1000 MHz
- Peak-to-peak bandwidths up to 75%
- Linearity from ±1.0%

Modeł Number	Center Frequency (MHz)	Linear Bandwidth (MHz, Min.)	Sensitivity (mV, MHz)	Rise Time (ns, Max.)	Linearity (±%, Max.)
FMDM-21.4/4-5	21	4	1000	150	2
FMDM-30/6-8	30	6	1000	120	2
FMDM60/10-15	60	10	250	75	2
FMDM-160/35-15	160	35	100	30	3
FMDM-160/50-25	160	50	20	17.5	5
FMDM-300/100-20	300	100	20	20	2.5
FMDM-1000/300-70	1000	300	10	5	5

All models are available with a variety of custom options, including: custom frequencies, special packaging, gain and phase tracking, and integrated assemblies combining multiple functions.

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instant Phase Limiting Amplifiers

- Operating frequencies from 10 to 600 MHz
- Standard models up to 70 dB dynamic range
- Maximum phase deviation as low as ±1.5°

	1.00					cross-reference
Model Number	Center Frequency (MHz)	Bandwidth (3 dB) (MHz, Min.)	Dynamic Range (dB, Min.)	Phase Change (±Deg., Max.)	Output Power (dBm, Min.)	guide
LCPM-30/10-70	30	10	-70 to 0	4	10	
LCPM-60/20-70	60	20	-70 to 0	5	10	A CONTRACTOR OF A CONTRACTOR OFTA CONTRACTOR O
LCPM-60/14-65	60	14	-70 to -5	2.5	10 👝	
LCPM-160/40-65	160	40	-70 to -5	5	10	MITER
LCPM-160/40-70	160	40	-65 to 5	3	10	M/N LCPM and
LCPM-300/50-55	300	50	-55 to 0	5	3	FREQ. 30 MHz
LCPM-500/100-45	500	100	-45 to 0	5	3	751346

Variable Gain Control Linear Amplifiers

- Operating frequencies from 21 to 850 MHz
- Standard models up to 75 dB of gain control range

Model Number	Center Frequency (MHz)	Bandwidth (3 dB) (MHz, Min.)	Dynamic Range (dB, Min.)	Noise Figure (dB, Max.)	P. Out @ 1dB Compr. (dBm, Min.)
VGC-7-30/10	30	10	-80 to -10	4	10
VGC-7-60/20	60	20	-85 to -10	6	10
VGC-7-70/10	70	10	-60 to -10	4	10
VGC-6-70/20	70	20	-50 to +10	5	10
VGC-7S-140/40	140	40	-75 to -10	7	10
VGC-6-160/40	160	40	-65 to -5	6	1
VGC-7-250/100	250	100	-70 to -10	6	10
VGC-4-720/100	720	100	-40 to 0	6	0
VGC-4-850/100	850	100	-40 to 0	6	0

Automatic Gain Control Linear Amplifiers • Operating frequencies from 21 to 850 MHz • Standard models up to 75 dB of gain control range

Model Number	Center Frequency (MHz)	Bandwidth (3 dB) (MHz, Min.)	Output Power (dBm, Min.)	Power Variation (dB, Max.)	Dynamic Range (dBm, Min.)
AGC-7P-30/15	30	15	10	2	-60 to +5
AGC-8-70/20	70	20	10	2	-75 to 0 🖉
AGC-6-70/30	70	30	3	2	-65 to -5
AGC-6-140/30	140	30	4	2	-65 to -5
AGC-4S-140/55	140	55	5	2	-40 to 0
AGC-5S-370/100	370	100	5	2	-60 to -10
AGC-5-387/175	387.5	175	-3	1	-60 to -15

For available options, custom design information, technical questions, or any additional information, please contact Boris Benger at (516) 436-7400, extension 140.



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INFO/CARD 13

RF calendar

August

3		
	14-18	IEEE EMC Symposium
		Atlanta, GA
		Fax: (310) 371-5268.
	21-23	RF Expo East
		Baltimore, MD
		Information: Argus Trade Shows, 6151 Powers
		Tel: (800) 828-0420, ext. 323.
	27-31	Surface Mount International '95
		San Jose, CA
		Information: Yolanda White. Tel: (415) 905–4994.
Septe	mber	
	5-7	International Conference on 100 Years of Radio
		London, UK
		IEE, Savoy Place, London WC2R 0BL UK.
		Tel: 071 344 5477. Fax: 071 497 3633.
	20-22	17th Annual Biozoalastria Daviasa Conference
	20-22	Kansas City, MO
		Information: Components Group, Electronic Industries
		Association, 2500 Wilson Boulevard, Arlington, VA
		22201-3034. 1et. (103) 301-1300. Pax. (103) 301-1301.
	26-28	Sixth International Conference on Radio Receivers
		and Associated Systems
		Information: RRAS'95 Secretariat, IEE Conference
		Services, Savoy Place, London WC2R 0BL UK.
		Tel: +44 (0) 71 344 5477. Fax: +44 (0) 71 497 3633.
	27-29	6th IEEE International Symposium on Personal.
		Indoor and Mobile Communications
		Toronto, Canada Information: University of Terento, Dent. of Floatnicel and
		Computer Engineering, 10 Kings College Rd., Toronto.
		Ontario M5S 1A4, Canada; Tel: (416) 978-3652.
Octob	er	
	3-11	TELECOM 95
		Geneva, Switzerland
		Information: International Telecommunication Union, Place des Nations, CH-1211 Conous 20, Suritzarland, Tele
		41 22 730 5111. Fax: 41 22 733 7256.
	8-11	1995 Wireless Circuits, Interconnection, and
		Assembly Workshop
		Tucson, AZ
		Information: Wireless Workshop, 100 S. Roosevelt Avenue, Chandler, AZ 85226
		Tel: (602) 961–1382. Fax: (602) 961–4533



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	NO.	TEMEX	PASS	BAND		STOPE	AND)	LOSS	RIPPLE	ULT. REJ.	TERM.(Rp//Cp)
	POLES	P/N	dB	[‡] KHz	dB	[‡] KHz	dB	†KHz	dB	dB-MAX	dB-MIN.	OHM/PF
	2	TE5000	3	3.75	20	18.0			2	1.0	50	1800//+4
	4	TE5010	3	3.75	30	14.0				2.0	60	1500//+3
N	6	TE5020	6	3.75	60	12.5				2.0	70	1500//+3
	8	TE5030	6	3.75	60	10.0	90	12.5		2.0	80	1500//+3
	2	TE5040	3	6.50	20	30.0			1	1.0	50	2700//0
	4	TE5050	3	6.50	30	15.0			2	2.0	75	3100//0
	6	TE5060	6	6.50	60	19.5				2.0	90	3100//0
	8	TE5070	6	6.50	60	13.0	80	17.5		2.0	100	3100//0
	2	TE5080	3	7.50	20	35.0	1.	1000		1.0	50	3000//0
	4	TE5090	3	7.50	30	17.5	334			2.0	75	3300//0
	6	TE5100	6	7.50	60	22.5	400-			2.0	90	3300//0
	8	TE5110	6	7.50	60	15.0	80	20.0		2.0	100	3300//0
	2	TE5120	3	15.0	20	70.0				1.0	35	5000//-1
1000	420-00	TE5130		15.0	30	35.0				2.0	60	5000//-1
	6	TE5140		15.0	60	45.0			2	. 2.0	90	5000//-1
	8	TE5150		15.0	60	30.0	80	40.0	3	2:0	100	5000//-1

	14 101	TO SHALL M	2							50 m		
	NO.	TEMEX	PASS	SBAND	STO	PBAN	D		LOSS	RIPPLE	ULT. REJ.	TERM.(Rp//Cp)
1	POLES	P/N	dB	[±] KHz	dB	±KHz	dB	*KHz	dB	dB-MA)	dB, MIN.	OHM/PF
	2	TE5180	3	3.75	15	12.5			2.3	1.0 (50	850//+6
	4	TE5190	3	3.75	30	12.5			3	2.0	70	850//+5
	6	TE5200	6	3.75	60	12.5			46	2.0	90	850//+5
	8	TE5210	6	3.75	60	10.0	80	12.5	-5	2.0	100	850//+5
100	2	TE5220	3	6.50	15	20.0			201	1.0	- 50	1300//+2
	4	TE5230	3	6.50	30	22.5			3	2.0	70	1400//0
-	6	TE5240	6	6.50	60	22.5		(Come)	4	2.0	90	1400//0
	8	TE5250	6	6.50	-60	17.5	80	22.5	4	2.0	100	1400//0
N.	2	TE5260		7.50	15	25.0	-	100-17	2	1.0	50	1500//0
	4	TE5270	3	7.50	30	25.0	1 25		3	2.0	70	1600//0
N	6	TE5280	6	7.50	60	25.0		and the second	4	2.0	90	1600//0
	8	TE5290	6	7.50	60	20.0	80	25.0	4	2.0	100	1600//0
	2	TE5300	3	15.0	15	50.0	North	1. 1. 1. 1. 1.	2	1.0	45	3000//0
	4	TE5310	3	15.0	30	45.0	n new	NUSSE	3	2.0	60	3000//-1
W.	6	TE5320	6	15.0	60	45.0	4048		3	2 ₈ 0	90	3000//-1
œ.	8	TE5330	6	15.0	60	33.0	80	45.0		2.0	100	3000//-1
		and an other set.	STREET, ST. L.	A DESCRIPTION OF TAXABLE PARTY.	LOUBER MERE	and the second second		and the second second		and the second second	and the second se	

	NO.	TEMEX	MODE	PASS	BAND	STC	PBAND	LOSS	RIPPLE	ULT. REJ.	TERM.(Rp//Cp)
Z	POLES	P/N		dB	tKHz	dB	tKHz	dB	dB-MAX	dB-MIN.	OHMIPE
H	2	TE9420	3nOT	3	3.75	18	16.0	3	1.1	40	2000//-1.0
	1004 340	TE9310	3-OT	3	3.75	30	12.5	-3	08. L. C	70	2000//-1.0
	2	TE7420	3-OT	3	7.50	18	28.0	2		40	3000//-1.0
0	4 - 1	TE7430	3-OT		7.50	40	30.0	3		70	3000//-1.0
	2	TE7440	3-OT	3	15.0	NO 15	47.0	2	1.1	40	8000//-1.5
5	4 and	TE7450	3-OT	1.13	15.0	30	50.0	3		70	8000//-1.5
Z	2	TE7730	FUND	3	15.0	15	50.0	2	Sheet She	40	1100//+1.5
1.42	4	TE7740	FUND	3	15.0	40	60.0	3	A DO MAR	70	800//+1.0

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RF courses

Introduction to RF & Wireless Engineering

October 10-13, 1995, Atlanta, GA Principles of Modern Radar November 6-10, 1995, Atlanta, GA Information: Continuing Education, Georgia Institute of Technology, Atlanta, GA 30332-0385. Tel: (404) 894-2547.

Microwaves and RF Measurements & Applications

October 2-5, 1995, Washington, DC Information: University Consortium for Continuing Education, 16161 Ventura Boulevard, M/S C-752, Encino, CA 91436. Tel: (818) 995-6335. Fax: (818) 995-2932.

Kalman Filtering

August 28-31, 1995, Los Angeles, CA Wavelet Transform Applications to Data, Signal, Image and Video Processing

September 11-15, 1995, Los Angeles, CA Information: UCLA Extension, Engineering Short Courses, 10995 LeConte Ave., Ste. 542, Los Angeles, CA 90024. Tel: (310) 825–1047. Fax: (310) 206–2815.

DSP Without Tears

September 20-22, 1995, Washington, DC

October 9-11, 1995, Dallas, TX

Information: Z Domain Technologies, Inc., 325 Pine Isle Court, Alpharetta, GA 30202. Tel: (800) 967–5034, (404) 587–4812. Fax: (404) 518–8368. **Global Positioning System: Principles and Practice** September 11-14, 1995, Washington DC PCS: A Telecommunications Revolution October 16-20, 1995, Washington, DC Antennas and Antenna Systems: Practical Design, Implementation, and Testing October 23-26, 1995, Washington, DC Wireless Telecommunications: An Introduction November 13-15, 1995, Washington, DC **Digital Transmission Systems** November 13-17, 1995, San Diego, CA Video Transmission and Broadcasting Via Satellite November 20-21, 1995, Washington, DC Information: The George Washington University, Continuing Engineering Education, Academic Center, Room T-308, 801 22nd Street, N.W., Washington, DC 20052. Tel: (202) 994-6106 or (800) 424-9773.

Fax: (202) 872–0645.

Wireless Communication Networks

August 24-25, 1995, Berkeley, CA Advanced Metallization Conference October 3-5, 1995, Portland, OR

October 24-25, 1995, Tokyo, Japan Information: Continuing Education in Engineering, University Extension, University of California, 2223 Fulton St., Berkeley, CA 94720. Tel: (510) 642-4151. Fax: (510) 643-8683.



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- Simulate circuit performance in response to a steady-state time-domain signal using impulse, step, pulsed carrier or userdefined stimuli.
- · Synthesize matching networks with Circles, an interactive Smith[®] Chart utility.
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- "Black box" elements (two-terminal impedance specified by resistance and reactance; two-terminal one port specified by admittance, impedance or reflection coefficient; three-terminal two-port specified by admittance, impedance or S parameters)
- · Controlled sources (current-controlled current, current-controlled voltage, voltage-controlled current, voltage-controlled voltage)
- Lossy capacitors, inductors, coaxial cables and transmission lines
- Transformers (ideal two- and three-winding types, specifiable in terms of
- turns ratio or impedance)

Technical Specifications for ARRL Radio Designer 1.0 Analysis:

9

Maximum number of nodes per circuit block*	250
Range of node-number values	0 through 99
Maximum number of ports per circuit block	30
Maximum number of frequency steps	512
Maximum number of statistical histograms	20

The number of circuit blocks allowed depends on their complexity; generally, 50 or more circuit blocks may be defined in a single ARRL Radio Designer netlist.

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- . Chain (ABCD), hybrid (H), inverse hybrid (G), gain, voltage gain, and stability parameters for two-port networks;

 Magnitude of reflection coefficient, phase of reflection coefficient, VSWR and return loss parameters for one-port networks:

- · Gain, gain matching and noise parameters; and
- · Complex S, Y, Z, H, G, chain (A), gain matching, noise matching and voltage probe parameters.

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 Rectangular and polar graphs—onscreen and via any Windows[™] compatible printer, in the colors, fonts and line weights you specify

 Tables—onscreen, in file form and via any Windows[™] compatible printer

Minimum system requirements for ARRL Radio Designer 1.0:

- 386, 486 or Pentium™ IBM PC or 100% compatible (math coprocessor strongly recommended)
- 8 Mbytes of RAM
- Microsoft Windows[™] 3.1 or higher
- 3.5-inch, high-density floppy drive
- hard disk with at least 5 Mbytes of free space Mouse or equivalent pointing device

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NIST Seeks Input for Standards Directory

The National Institute of Standards and Technology is updating its popular directory, *Standards Activities of Organizations in the United States*, for the first time in four years. The 1995 edition will feature information on groups outside the formal framework, such as consortia, user groups and ad hoc task forces. Standards groups may contact the publication contractor, R.B. Toth Associates, at (703) 329-0658.

Commercial Remote Sensing Satellite System Planned

Geophysical & Environmental Research Corporation (GER) has announced its GEROS project, a system of up to six remote sensing satellites that will provide on-line images and analysis for agricultural production, environmental protection, forestry and land management, disaster response, surveillance and other uses. GER satellites and ground systems will be built by various contractors using the company's technology and proprietary analysis algorithms. The satellites will obtain data in the visible and invisible light ranges, radar and emitted heat. SpaceVest of Reston, Virginia, is providing the startup capital for the GEROS project.

Solar Car Race Uses Satellite and Cellular Technology

Hughes Network Systems (HNS), Delco Electronics and Electronic Data Systems (all General Motors companies), have developed a location and communication system that was used in Sunrayce 95. The race is a biennial collegiate competition held this year on June 20-29, with teams racing 1150 miles from Indianapolis, Indiana to Golden, Colorado. 40 schools qualify for the race, out of approximately 65 applicants. EDS maintains the Sun-

Conference News

Call for Papers: European Frequency and Time Forum - Precise measurement of time and frequency is the focus of the European Frequency and Time Forum (EFTF), to be held March 5-7, 1996 in Brighton, U.K. Papers are invited which address important topics in time measurement and precise time and frequency applications: piezoelectric materials, oscillators, filters, frequency standards, synchronization systems, frequency synthesis, metrology, navigation, telecommunications and instrumentation. Authors should submit their intention to submit a paper immediately, and will receive instructions for a one-page summary. Send the proposal to: 10th European Frequency and Time Forum, Attn: Mrs. L.J. Hudson, EFTF Secretariat, IEE Conference Services, London WC2R 0BL, U.K. The conference language is English.

GaAs Man Tech Conference Drops U.S. Citizenship Requirement — Beginning with the 1996 conference in San Diego, the Conference on Gallium Arsenide Manufacturing Technology will be open to participants from around the world and U.S. citizenship will no longer be required to attend. The 10-year-old organization sponsoring the event will also expand its governing committees to include international representation. For more information, contact Publicity Chair Dave Miller at (201) 539-5500, Technical Program Chair James Oakes at (508) 470-9779, or Conference Chair Neal Mellen at (505) 822-8801, ext. 236.

ARFTG Call for Papers — Papers are invited for the Testing for Fall 1995 Automatic RF Techniques Group conference. The conference theme is: Testing for Wireless Applications. Topics sought include methods for reducing testing time, testing cost and high confidence. This includes on-wafer testing, fixture characterization and correlation of large signal RF to DC test parameters. Presentations are informal, 20 minute talks. Authors are requested to submit two copies each of a onepage abstract and a 500 to 1000 word summary, including illustrations, by August 28, 1995. Proposals should be sent to the Technical Program Chairs: Dr. Mike Golio and Dr. Dave Halchin, Motorola, MS EL-609, 2100 E. Elliot Road, Tempe, AZ 85284. Tel: (602) 413-5947, fax: (602) 431-4453, email: m.golio@ieee.org.

rayce Communications Center, Delco is providing audio and navigation systems for location information (based on support vehicle location), and HNS' dual-mode cellular phones and Direct- PC^{TM} high speed digital service provide communications.

Grocery Warehouse Benefits from Wireless Inventory Management

Smart and Final, the West's oldest and largest grocery retailer, reports increased operator productivity and a 10 percent increase in warehouse space utilization, accomplished by installing a RF inventory management system called Priya, from Motek Information Systems. Replacing a mainframe inventory system that could only be updated every 12 hours, the RF system provides real-time information on availability of slots for newlydelivered pallets of goods. Smart and Final estimates that it will get two or three more years' service from a warehouse that was previously considered to be at capacity.

NASA Develops Simplified Digital Down-Converters

NASA researchers at the Jet Propulsion labortory have developed a technique where the high-speed number controlled oscillators (NCOs) and mixer-multipliers used in a typical digital downconverter are replaced with multiplication coefficients of finite-impulse-response (FIR) filters. This simplification depends on particular choices of operating frequencies.

The combined functions of NCO and mixers are equivalent to multiplication of the input signal samples by time-varying coefficients. Implementation of the FIR filter solution in the general case would require updating coefficients on every clock cycle. However, if the local oscillator frequency is restricted to integer multiples of the output clock frequency ($f_L = nf_0$), then the local oscillator coefficients that must be incorporated into the FIR coefficients are constants, each successive cycle representing the same phase of the signal.

The technique is less restrictive if the FIR filter has coefficient memory. In this case, a series of repeating coefficients can effectively multiply the number of usable frequencies ($mf_L = nf_0$), where m is the number of available coefficient memories.

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Business Briefs

Varian's Electron Devices Business Sold, Becomes Communications & Power Industries — Varian Associates has agreed to sell its Electron Devices business to Leonard Green & Partners, L.P. for approximately \$200 million in cash and assumption of certain liabilities. The Electron Devices operation has net assets of approximately \$120 million and annual sales of about \$250 million. Varian's other businesses are not involved in the sale. The group manufactures vacuum tubes, amplifiers and power supplies.

Dynair Acquired By Osicom Technologies — Dynair Electronics, a privately held company, has been acquired and will become a subsidiary of Osicom Technologies, joining other Osicom communications-related subsidiaries Meret Optical Communications and Catel Telecommunications. Dynair manufactures digital and analog switching and distribution systems for video, broadcasting, imaging, surveillance and information displays.

AMP and M/A-COM Close Merger — Shareholders of M/A-COM Inc. approved a merger proposal with AMP Incorporated on June 30, 1995, and the merger has been completed. Under the terms of the merger, M/A-COM stockholders will receive 0.280 shares of AMP common stock for each M/A-COM share. Richard P. Clark has been named as both president of M/A-COM and as divisional vice president of AMP Global Wireless Products Group, under which M/A-COM operates as a subsidiary.

Merix to Buy Hewlett-Packard PC Board Operation — Merix Corporation, formerly the printed circuit board division of Tektronix, and Hewlett-Packard Company have signed a memorandum of understanding for purchase of HP's Loveland, Colorado circuit board fabrication operation for a price estimated at \$23.6 million. Initially, Merix will lease the 120,000 square foot facility for five years, and will produce boards for HP as its major customer.

Dover Acquires AT&T Division — Vectron Technologies, Inc., a subsidiary of Dover Technology International, has acquired all of the assets of the AT&T Microelectronics Frequency Control Products group. The AT&T group has supplied piezoelectric based oscillators to various divisions of AT&T for more than 40 years, and has recently expanded its markets to include OEM sales to other telecommunications companies. The operation will be moved from its current location in Andover, MA to a new 43,000 sq. ft. facility in Hudson, NH.

Contracts

RF Power Products Announces \$1.3M Contract — RF Power Products has received a one-year agreement for its RF power generators from Mattson Technology valued at approximately \$1,300,000. Mattson will use the power generators in their photoresist strippers, rapid thermal processing and chemical vapor deposition systems used in the semiconductor industry. RF Power Products makes power generators and peripheral products for the semiconductor, analytical instrument, commercial coating and flat panel display industries.

Microdyne to Supply Telemetry Receivers to the Navy — Microdyne Corporation, Aerospace Telemetry

Telxon and The Shams Group in Medical Partnership — A joint marketing agreement has been announced between Telxon and The Shams Group (TSG), which will integrate Telxon's pen-based wireless computers into TSG's MEDITECH healthcare information systems. Wireless connectivity allows real-time updating of patient records and transmission of data directly to the point of care.

COMET Has New Address — COMET North America is moving to larger offices, to cope with its substantial growth. The new address is 89 Taylor Avenue, Norwalk, CT 06854, tel. (203) 852-1231, fax. (203) 838-3827.

PTI Adds Manufacturing Space — Piezo Technology. Inc. announces an expansion of its manufacturing facility with 5000 additional square feet of space. PTI makes filters, crystal oscillators and resonators.

RF Industries Completes Move — **RF** Industries, Ltd. has moved to a new location at 7610 Miramar Road, San Diego, Calif. 92126. Telephone and fax numbers remain the same, (619) 549-6340 and (619) 549-6345, respectively

Richardson Signs Up Huber+Suhner — Richardson Electronics has been named national distributor in the U.S. for Huber+Suhner's line of coaxial connectors, adapters, EMP protectors, antennas and RF components.

NEC Moves NEPOCTM Product Sales to California Eastern Laboratories — Sales of the NEPOC line of photocouplers, interrupters, fiber cptic links, photo transistors, photo diodes and detectors has been transferred from NEC Electronics, Inc. to California Eastern Laboratcries.

LNY Sales is U.S. Agent for Plessey Tellumat — Plessey Tellumat, South Africa, has signed an agreement with LNY Sales, Inc for exclusive sales of their low noise amplifiers for cellular, paging and satellite applications.

Spinner Coaxial Connectors Marketed by Precision Tube/Coaxitube — Exclusive U.S. importing and marketing rights for Spinner GmbH connectors have been assigned to Precision Tube Co./Coaxitube Division of Salisbury Md. The Spinner line features the Spinner-originated 7-16 connector, along with HN, N, C, SC and other types.

Femtosecond Systems Relocates — Femtosecond Systems, a manufacturer of precision oscillator noise measurement equipment, has a new address: 690 Arbutus St., Golden, CO 80401, tel: (303) 462-0799, fax: (303) 462-0766.

Division, has announced a major contract to provide nearly 100 of its new VMR-2000 VME bus controlled telemetry receivers and VMC-2001 Pre-Detection and Post-Detection diversity combiners, plus several telemetry signal simulators, to be used in an unidentified U.S. Navy program. The VME bus equipment will reduce the space requirements of previous rack-mount equipment. *RF*

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RF industry insight

High-End Test Equipment Reflects New Communications Activity

By Andy Kellett Technical Editor

If you haven't started seeing advertisements and new product releases for test equipment designed for installation and repair of systems such as GSM, various PCS systems and the new cable services, you soon will. While thousands of specialized test-sets will be manufactured to assist the armies of technicians it will take to install and maintain these new systems, the test equipment used in research and development is also changing to fit the new systems.

Complex Measurements

The new systems are complex. Complex (literally) modulation schemes such as $\pi/4$ DQPSK and GMSK have replaced modulations such as plain old FM; and channels are assigned both in time and frequency - the Digital European Cordless Phone (DECT) system assigns users to one of eight time slots, in addition to assigning them a frequency. "Along with complexity comes the need for more sophistication in test equipment," says Lynn Stewart, Market Development Manager for Wireless Communications at Hewlett-Packard's Microwave Instruments Division, "we look at signals in different ways than we have in the past."

According to Stewart, some of the most important measurements, particularly in the new wireless communications systems, are power measurement in both the frequency and time domain, and transmitter on/off times. Tom Brinkoetter, Marketing Manager at Tektronix pointed to those two measurements as important as well. Brinkoetter says looking at adjacent channel power is very important to manufacturers of multi-channel wireless systems, particularly digital systems. Brinkoetter adds that measuring transmitter on/off times is important to ensure transmitters in time-multiplexed systems don't interfere with each other, but also to make sure they follow the correct on/off profile to minimize sidebands, "again it's back to the adjacent channel power issue," says Brinkoetter.

The complex interplay of frequency domain and time domain specifications has prompted equipment manufacturers to make boxes capable of quickly and easily looking at signals in both domains.

Measurement Precision

While complex communications systems have caused equipment manufacturers to make their equipment more complex, the steadily improving performance of individual components has pushed up the basic performance of test equipment as well.

Customers are requesting lower noise in signal sources and improved performance from analyzers as the devices they test become more linear, have lower loss and have higher dynamic range. Brinkoetter points to measuring the response of diplexers for PCS use. A diplexer may see a +30 dBm transmit signal and a -130 dBm receive signal at its input, says Brinkoetter, "...so the rejection has to be well over 100 dB, and that requires the network analyzer to have that kind of sensitivity."

Customers for the Rohde & Schwarz FSE series spectrum analyzers, (distributed by Tektronix in the U.S.), have found the instrument's high dynamic range very useful says Brinkoetter, "they can see sidebands below specs, at levels close to the noise, without having to use a long sweep time."

Good calibration practices are becoming more important. The effect of bad adapters, connectors and terminations can be ten percent or more of a device's measured return loss, particularly if the device has low insertion loss, says Ken Harvey, Product Marketing Manager at the Wiltron Company. "I can find on almost every bench a connector or adapter that will cause a measurement to be out of spec," he says. To make it easier to calibrate all the connectors, adapters, etc. in a test set-up, Harvey says Wiltron's 54100 scalar analyzers include a precision return loss mode for use with a piece of precision air-line, which allows the person performing the test to find bad components and calibrate out their effects.

Manufacturing Measurements

Changes in manufacturing are also reflected in test equipment. ISO 9000 has prompted manufacturers to get the uncertainty of their measurements under control says Harvey, which is another reason to be sure of system calibration.

The manufacturers who use RF test equipment want to test as many devices as possible, so test speed is also important. "What we've seen in manufacturing is they tend to wrap R&D equipment in software," says Tektronix' Brinkoetter. The purpose of this software is to automate the testing process. With the software available with many instruments, procedures which took an hour to perform can be set-up and performed at a touch of a button.

Not only set-up times, but the times of the measurements themselves are being reduced. The IEEE-488.2 control bus standard is a speedier version of the old IEEE-488 standard, and using this bus, Wiltron has demonstrated analyzers capable of sending data to a computer in almost real time. Wiltron's Harvey says demand for fast test times helped drive their design for a very fast-stepping phaselocked synthesizer.

Conclusion

New communications systems are prompting test equipment manufactures to include more complex measurements in their boxes, tighter specs cause them to increase precision, and manufacturing is encouraging faster, easier testing procedures. RF

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RF synthesizers

Dual PLL IC Achieves Fastest Lock Time With Minimal Reference Spurs

By William O. Keese National Semiconductor

The LMX233XA dual PLLs are designed for use in dual-synthesizer wireless designs. With a maximum frequency of 2.5 GHz, the series supports designs where fast frequency lock times and minimal reference spurs are crucial.

PLL frequency synthesizers are a vital component in wireless applications such as digital cellular phones, pagers, and set-top boxes. Applications that include dual down converters with an RF and IF stage make use of two PLL frequency synthesizers to generate separate frequencies for each stage. Full duplex systems, such as AMPS, need two RF synthesizers to generate both receive and transmit local oscillators simultaneously. Dual PLL chips, which supply both the RF and IF or two RF LOs, excel in dual synthesizer designs because of their reduced parts count, lower power consumption, and smaller board space requirements. The block diagram for the dual PLL chip is shown in Figure 1.

Like single PLL ICs, dual PLLs ICs must offer fast switching times and a minimum of spurious output and phase noise. The LMX233XA series ICs, the newest members of the PLLatinum family from National Semiconductor (Santa Clara, CA), offer a frequency lock time that's the fastest in the industry, minimal reference spurs, and no dead-zone.

The LMX233XA cuts lock time by 35 percent by using its patented Fastlock[®] technique. Fastlock shifts the loop filter's pole and zero corner frequencies while maintaining the PLL's gain/phase margin characteristics, using only one external resistor.

Fastlock Implementation

Figure 2 shows a conventional PLL configuration consisting of a high-stability crystal reference oscillator, a frequency synthesizer, a voltage controlled oscillator (VCO) and a passive loop filter. (A passive filter is preferred over a higher order filter because of its simplicity, low cost, and reduced phase noise.) The frequency synthesizer includes a phase detector, a current mode charge pump, and programmable reference (R) and feedback (N) frequency dividers.

In conventional PLL design, the tuning resolution of the PLL is set by the R counter dividing the crystal reference signal down to some reference frequency f_r , which is input to the phase detector. The phase detector compares it with f_p, the feedback signal, obtained by dividing the VCO frequency down by the N counter. The phase detector's current-source feeds into the loop filter, which converts the charge into the VCO's control voltage. The phase/frequency comparator's function is to adjust the voltage presented to the VCO until the feedback signal's frequency and phase match the reference signal. When this "phase-locked" condi-tion exists, the VCO's frequency will be N times that of the comparison frequency.

Increasing the value of the N counter by one will cause the phase comparator to initially sense a frequency error between the reference and feedback signals The feedback loop responds by shifting the VCO frequency to N+1 times the reference signal. The VCO's frequency has in effect increased by the



Figure 1. Dual PLL chips, which supply both the RF and IF stage frequency synthesizers.



Figure 2. A conventional PLL configuration.

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POS-300	150-280	-100	-30	18	13.95
POS-400	200-380	-98	-28	18	13.95
POS-535	300-525	-93	-26	18	13.95
POS-765	485-765	-85	-21	22	14.95
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Figure 3. A linear control system model of the phase feedback for a PLL in the locked state.



Figure 4. A Bode plot of the magnitude and phase of G(s)H(s) for a stable loop is shown by the solid trace.

minimum tuning resolution of the PLL. The transition rate to the new operating frequency is determined by the closed loop gain and the stability criteria:

Open Loop Gain = H(s)G(s) =
$$\frac{\theta_i}{\theta_e}$$
 (1)

$$=\frac{K_{pd}Z(s)K_{vco}}{Ns}$$

$$Z(s) = \frac{s(C2 \cdot R2) + 1}{s^2(C1 \cdot C2 \cdot R2) + sC1 + sC2}$$
(2)

$$\Gamma 1 = R2 \cdot \frac{C1 \cdot C2}{C1 + C2}$$
(3a)

$$T1 = R2 \cdot C2 \tag{3b}$$

$$\left| G(s) \cdot H(s) \right|_{s=j\omega} =$$
 (4)

$$\frac{-K_{pd} \cdot K_{vco}(1+j\omega \cdot T2)}{\omega^2 C1 \cdot N(1+j\omega \cdot T1)} \cdot \frac{T1}{T2}$$

$$(\omega) = \tan^{-1}(\omega \Gamma 2) \tag{5}$$

$$\tan^{-1}(\omega T1) + 180^{\circ}$$

A linear control system model of the phase feedback for a PLL in the locked state is shown in Figure 3. The open loop gain is the product of the phase comparator gain (K_{ϕ}) , the VCO gain $(K_{\nu co}'s)$ and the loop filter gain Z(s) divided by the gain of the feedback counter modulus (N) (equation 1). The complex impedance of the passive loop filter used is given in equation 2. The time constants which determine the

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pole and zero frequencies of the filter transfer function are defined in equations 3a and 3b. The third order PLL open loop gain can be calculated in terms of frequency, ω , T1 and T2 and K_{ϕ}, K_{vco}, and N (equation 4). From equation 4, the phase term will be dependent on the single pole and zero such that the phase margin is determined in equation 5.

A plot of the magnitude and phase of G(s)H(s) for a stable loop is shown by the solid trace in Figure 4. The parameter ϕ_p shows the amount of phase margin that exists at the point the gain drops below zero (the cutoff frequency ω_p of the loop). In a critically damped system, the amount of the phase margin would be approximately 45 degrees. To minimize lock time, the cutoff frequency of the loop ω_p should be just wide enough to suppress the PLL's reference frequency spurs to a tolerable level.

In Fastlock, the cutoff frequency is redefined as $\omega_{p}' = 2\omega_{p}$, the loop response time would be approximately halved. Because the filter attenuation at the comparison frequency also diminishes, the spurs would have increased by approximately 6 dB. With Fastlock, however, the higher spur levels and wider loop filter conditions exist only during the initial lock-on phase, which is just long enough to realize the faster lock-on time. In effect, the curve of Figure 4 slides over to the cutoff frequency illustrated by the dotted line, without affecting the relative open loop gain and phase relationships.

To maintain the original gain/plase relationship at twice the original cutoff frequency, other terms in the gain and phase equations 4 and 5 will have to compensate by the corresponding 1/w or $1/\omega^2$ factor. Examination of equations 3 and 5 indicates the damping resistor variable R2 could be chosen to compensate the w terms for the phase margin. This implies that another resistor of equal value to R2 will need to be switched in parallel with R2 during the initial lock period. In addition, the magnitude of the open loop gain, G(s)H(s) must be set equal to zero at $\omega_p{'}{=}2\omega_p{\cdot}~K_{\nu co},~K_\phi,~N,~or$ the net product of these terms can be changed by a factor of 4, to counteract the ω^2 term present in the denominator of equation 3. While altering K_{vco} would be difficult at best, both K_p and N are readily avail-able in a PLL IC. K_{ϕ} was chosen to complete the transformation because it can be readily switched between 1× and



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design.

 $4 \times$ values by increasing the charge pump current from 1 mA in the standard mode to 4 mA in Fastlock.

(Changing the N gain term could also have been chosen to accomplish our objective. In fact, doing so causes the PLL's reference frequency to be pushed over in the reference domain along with the loop cutoff frequency. However, changing N also means changing the R counter value by the same factor, and while this is feasible, it introduces fractional counter techniques along with all the associated problems of the approach, as N/4 may no longer be an integer.)

Circuit Implementation

The LMX2335's Fastlock scheme is shown in Figure 5. When a new fre-

quency is loaded the charge pump receives an input to deliver four times the normal current per unit phase error while an open-drain NMOS on-chip device switches in a second R2 resistor to ground. The user calculates the loop filter component values for the normal steady-state considerations. The device configuration ensures that as long as a second identical damping resistor is wired in appropriately, the loop will lock faster without any additional stability conditions. Once locked onto the correct frequency, the PLL returns to standard low noise operation. This transition does not affect the charge on the loop filter capacitors and is synchronous with the charge pump output, creating a virtually seamless change between Fastlock and standard mode.



Figure 6. The LMX233XA deadzone elimination circuit.

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	LMX2330	LMX2331	LMX2332	LMX2335
Туре	RF/IF	RF/IF	RF/IF	RF/IF
	Dual	Dual	Dual	Dual
RF input				
- Main PLL	2.5 GHz	2.0 GHz	1.2 GHz	1.1 GHz
RF Input				
-Aux PLL	510 MHz	510 MHz	510 MHz	1.1 GHz
Prescaler				
-Main PLL	32/33 or 64/65	64/65 or 128/129	64/65 or 128/129	64/65 or 128/129
Prescaler				
-Aux PLL	8/9 or 16/17	8/9 or 16/17	8/9 or 16/17	64/65 or 128/129
IDO Leakage	2.5 nA @ 85°C	2.5 nA @ 85°C	2.5 nA @ 85°C	5 nA @ 25 °C
Opr. Temp.	-40 to +85 °C	-40 to +85 °C	-40 to +85 °C	-40 to +85 °C
Vcc range	2.7 to 5.5 V	2.7 to 5.5 V	2.7 to 5.5 V	2.7 to 5.5 V
Icc (typ)	15 mA @ 3V	14 mA @ 3V	8 mA @ 3V	9 mA @ 3V
Icc pwrdown (typ)	1 μA @ 3V	1 μA @ 3V	1 μA @ 3V	1 μA @ 3V
Package	TSSOP 20	TSSOP 20	TSSOP 20	SO 16 - JEDEC
Typ. Applications	ISM (2.4 - 2.45)	DECT, DCS1800	GSM, IS-54	AMPS, NMT
	DECT, CATV	RCR-28, RCR-27	RCR-27	ETACS, CT-1
	WLAN	CATV	ISM (902-928)	CT-1+, CT-2
		and the second second		ISM(902-928)
Order #	LMX2330TM	LMX2331TM	LMX2332TM	LMX2335M
("X"=tape & reel)	LMX2330TMX	LMX2331TMX	LMX2332TMX	LMX2335MX
Production avail.	now	now	now	Q2CY95

Table 1. The LMX233x family

IS-54 Application Example

An LMX2335 was used in an IS-54 design with the following constraints: F_{vco} =900 MHz, K_v =20 MHz, and channel spacing=30 kHz. The PLL's device attributes were: K_{ϕ} =1mA/2 π , N= 30,000, F_{ref} =30 kHz, and F_o =3 kHz. The loop filter values used were: C1 = 1800 pF, R2 = 12 k, C2 = 0.012 μ F.

The circuit locked within 1 msec (\pm 1 kHz) for a frequency jump of 50 MHz, compared with 1.6 msec for the standard PLL lock time. A small frequency disturbance can result when switching back to normal operation after reaching steady-state. By switching out of Fastlock mode when the PLL has settled near the desired frequency tolerance, almost the entire 2× increase in lock time can be achieved.

Minimal lock time is not the only requirement for a PLL - low phase noise and low reference spurs are also necessary. A deadzone elimination circuit and an almost perfectly balanced charge pump allow the LMX233x to meet these requirements.

A deadzone can occur in certain PLL implementations as the error becomes infinitesimally small. The PLL circuit reaches the point, called the deadzone, where the current source pulse width becomes too narrow to control and collapses to zero. A zone of phase error corrections will result which receive no responding current flow.

The LMX233XA deadzone elimina-

tion circuit (Figure 6) ensures that the charge pump current sources have actually responded to the phase comparator output signals (PU and PD) before activating the phase comparator reset logic. Both the pump up and pump down circuit always turn on, so the net difference, not the width of the pulses themselves, is the error correction signal. Because of the deadzone elimination circuit, the current pulses never collapse to zero allowing vanishingly small error correction pulses into the PLL loop filter in a controllable fashion. When the signal is out of lock, the corresponding pump-up or pumpdown pulse width increases. As the frequency error is minimized, the difference between the correction pulses becomes smaller, until the PLL becomes "phase-locked," where the sink and source currents are equal, and zero net charge is injected into the loop filter. The circuit is therefore able to make minimal error corrections, without having to generate a narrow pulse which is dominated by the turn-on time of the charge pump output transistors.

Reference spurs are minimized by virtue of the charge pump being almost perfectly balanced. The LMX233XA's manufacturing process yields physically identical current-generating structures for the pump-up and pump-down circuits, which ensures that the magnitudes of their current sources, as well as matching their turn-on and turn-off times. This matching minimizes the momentary pump up or down excursions on the charge pump line which are a major contributor to reference spurs.

Like the balanced charge pump currents, the deadzone elimination circuitry also works to minimize the spurs because the charge pump feedback signals allow the generators to be on only long enough to eliminate potential deadzone, without contributing any excess active pump time. Excess pump time adds directly to the up or down excursions on the charge pump line by the amount the absolute magnitudes of the current generators differ. Coupled with the balanced source and sink currents, the circuitry can be tuned to exactly the same magnitude for a minimal period of time and the reference spurs are correspondingly minimized. At less than -74 dBm, the LMX233XA's reference spurs are the lowest in the industry.

Lower reference spurs means less filtering is needed at the board level. The PLL loop filter bandwidth can be increased for the same amount of spurious rejection, which means faster lock times. Similarly, because the charge pump has negligible leakage current, no "sawtoothing" occurs in the VCO control voltage, which could also contribute to spurs. The loop filter can often be implemented with a second order filter, instead of more exotic filters, resulting in fewer components, and fewer headaches.

For more information on the LMX233x family of dual PLLs call (800) 272-9959. RF

About the Author

William O. Keese is a Senior **Applications Engineer at National** Semiconductor Corporation in Santa Clara. Keese is head of phase-locked loop applications in the Wireless Communications division and has designed synthesizers for a variety of cellular and cordless communications standards, such as GSM, IS-136, DECT and PHS. Keese received a double major in **Electrical Engineering and Materi**als Science from the University of California at Davis. He is currently completing his MSEE at UCD in **RF** and Microwave Engineering. He can be reached at 2900 Semiconductor Dr., M'S A-1500, Santa Clara, CA 95052-8090

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RF biasing

Low Dropout Current Source Protects Silicon MMICs and Transistors

By John V. Bellantoni Watkins-Johnson Co.

This 1994 RF Design Contest entry solves a problem often faced by RF designers concerned with both cost and power dissipation: is there a way to use low cost silicon devices over a wide temperature range without incurring any additional power dissipation in the bias circuitry? Here is a design that makes large voltage drops in amplifier bias circuits a thing of the past. Silicon transistors and MMIC amplifiers are widely used in RF applications where cost and simplicity are paramount concerns. Figure 1 summarizes the most popular biasing schemes for Si MMIC amplifiers [1]. Directly connecting the MMIC to the supply, as shown in Figure 1(a), is suitable only under laboratory conditions. The bias resistor shown in Figure 1(b) is a more practical method.



Figure 1. (a) Fixed Collector Voltage Bias Circuit, (b) Collector Bias Stabilization Resistor Circuit, (c) Two-Transistor Current Source (D_1 is a transistor b-e junction) (d) Two-Transistor Active Bias Circuit (reprinted from Reference 1).

However a minimum of 3 volts is neeced across the resistor to maintain stability over temperature. That voltage drop can be reduced to 1.7 volts with the two-transistor designs given in Figure 1(c) and 1(d). The two-transistor circuits still increase power dissipation of a 5 volt Si MMIC amplifier circuit by 30 percent. In addition, the current supplied by the two-transistor design is sensitive to variations in the supply voltage.

The literature doesn't seem to contain any schemes for safely biasing transistor circuits close to their operating voltages. What's needed is a simple way to provide a constant current – something that works over temperature, power supply, and load variations, without any significant voltage drop from supply line to device. Figure 2 is the author's low dropout current source (LDCS) that meets these requirements; it provides a constant current regardless of load impedance.



Figure 2. Low Dropout Current Source (LDCS) Circuit.

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Figure 3. MSA-0300 I-V characteristics (reprinted from Reference 2).

The current is sampled by R2, amplified by U1a, and then compared to a reference voltage by U1b. The feedback loop is closed by Q1. Equilibrium occurs when the voltage drop across R2, multiplied by the gain of U1a, equals the reference voltage. Since R5 = R6 and R3 = R4, the gain of the differential amplifier is R6/R4, and the current will be:

$$I_{s} = V_{ref} \frac{R4}{R2 \cdot R6}$$
(1)

where V_{ref} can be set by potentiometer R1, or by some other means. The potentiometer is a good choice to continuously vary the operating point, while fixed resistors or voltage references are best for specific bias points.

For proper circuit operation while operating from a single supply, the dual op amp must have an input common mode range that includes the positive rail. Suitable devices in this category are the Motorola MC33202, Maxim MAX492, and National LMC6482. Substituting other op amps can be tricky. For example, the common mode input range of a JFET device includes the positive rail, but a negative supply is required. On the other hand, low cost single supply op amps, such as the LM358, will not operate with input voltages near their positive supply voltage.

Performance of the LDCS is consistent and predictable. The prototype circuit, set to 35 mA, doesn't even move a tenth of a mA when the load is shorted out. Stability over temperature is essentially a function of V_{ref} , derived from V_{∞} . If V_{cc} is not stable over temperature or time, use an inexpensive adjustable shunt regulator, such as the LM431, to produce the reference voltage. An added advantage to using a shunt regulator is that a battery-derived V_{cc} can vary over a wide range without a significant change in

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Figure 4. Low Dropout Active Bias Circuit (LDBC).



Figure 5. VHF amplifier with LDBC.

current. Using an LM113 voltage reference, the current changed 9 percent – from 38 mA to 35 mA, when V_{cc} was decreased 50 percent, from 11.5 to 5.75 volts. Be careful not to set the supply voltage above 11.5 volts, since



Figure 6. Performance over temperature of the VHF amplifier with LDBC. $f_0=160$ MHz, $V_d=6$ Volts.

the MC33202 maximum rating is 12 volts (15 volts for the LMC6842).

The voltage drop across the circuit is due to R2 and Q1. At room tempera-



Figure 7. Two stage amplifier with LDCS.



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ture, dropout was 160 mV at 35 mA, 250 mV at 75 mA, and 400 mV at 150 mA. Most of the dropout is due to Q1; a more expensive device such as a 2N4276 will result in even lower dropout performance. To determine the minimum V_{cc} , add the dropout to the maximum device voltage. The maximum device voltage usually occurs at cold temperatures. An example is shown in Figure 3, which is the I-V characteristic of a MSA-0300 device [2]. From the -40° C curve in Figure 3, the device voltage at 35 mA is 5.5 volts. Adding 160 mV for the LDCS, and an extra 100 mV for design margin, only 5.76 volts is needed to bias the device over temperature.

For active bias of MMICs or discrete devices, switch the input pins at U1b, as shown in Figure 4. The MRF-553 VHF amplifier pictured in Figure 5

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Compex conpex conpersonal components Taunton Professional Parke, 238 Taunton Blvd. Medford, New Jersey 08055 (609) 596-9388 TAX (609) 596-3482 uses the design given in the data book [3]. However due to the added low dropout bias circuit (LDBC), performance over temperature, plotted in Figure 6, is rock solid, and efficiency for the entire circuit is just 1.5 percent less than the efficiency of the transistor.

Nearly endless variations to the LDCS circuit are possible. One of the author's favorite is the design shown in Figure 7, where two Si MMIC amplifiers are biased in series. The LT1129 in Figure 7 is a low dropout voltage regulator that provides overvoltage and reverse-bias protection, a temperature stable voltage reference for the current source, and requires only 3.3 µF for stability. The LDCS is placed between the MMICs. That way. the op amp inputs are well below V. so generic op amps, which are typically one third the cost of a rail-to-rail op amp, will work well. Whatever the application, the LDCS will keep a design on the road when low overhead clearance stops the rest. RF

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3. Motorola RF Device Data, Motorola, 1994, Rev. 5, pp. 2-374 to 2-377

About the Author



John V. Bellantoni is a Member of the Technical Staff at Watkins -Johnson Company, where he designs RF and microwave products for commer-

cial wireless applications and also for high performance military systems. He earned a BSEE from Worchester Polytechnic Institute and MSEE and Ph.D. from Cornell University. He can be reached at Watkins-Johnson Company, 3333 Hillview Ave., Pal Alto, CA 94304-1204. His e-mail address is john.bellantoni@wj.com, and he can be found on 80 through 10 meters CW as WB1ALZ.

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RF cover story

Low Cost 1000 Watt, 300 Volt RF Power Amplifier for 13.56 MHz

By Kenneth Dierberger, Advanced Power Technology, Bobby McDonald, UNI-WEST ENGINEERING Lee B. Max, Consultant

This article details the design, development, assembly and performance of a low cost, high-efficiency, 1000 watt, 13.56 MHz RF power amplifier (PA) operated from a 300 VDC supply, with an efficiency of 80 percent The PA is built around a "symmetric pair" of low cost RF power MOSFETs from Advanced Power Technology (APT). The transistors are from a new generation of high quality, commercial, HF/VHF, silicon, 900 V breakdown RF power MOSFETs in TO-247 packages.

Most transistorized RF power amplifiers operate from a DC to DC converter. This supply is usually low voltage, about 50 V, and requires a down regulator when operated from AC mains. This converter is a significant portion of the overall cost of the RF amplifier system.

As a result of IEC 555-2, all electronic equipment sold in Europe with a power draw of greater than 250 W will require power factor correction (PFC). The addition of a PFC preregulator to the system could add 50 to 100 percent to the cost of the power supply portion. The requirement for PFC is soon to follow in the USA and the rest of the world.

The use of new high voltage RF MOSFETs from Advanced Power Technology (APT) makes possible a new RF amplifier design which can be operated at 300 V, allowing for the direct use of a PFC regulated output, thus eliminating the DC to DC converter, reducing the cost of the RF amplifier system.

The new devices, like their predecessors, utilize the high performance of APT's Power MOS IV[®] technology and the "symmetric pair" package.

Amplifier Description

The amplifier is a 1000 Watt, 13.56 MHz design operating in class C with a 300 VDC power supply. Efficiency of



Small, simple power amplifiers for 13.56 MHz and other HF applications can be built with the APT "symmetric pair" MOSFETs, provided in low-cost standard TO-series packages. The ARF442/ARF443 units are pictured here.

the amplifier is 80 percent. The power amplifier is built around two "symmetric pair" of ARF444/ARF445 900 V RF power MOSFETs provided in TO-247 plastic packages. The devices are electrically identical, except that they are packaged in "mirror image" pairs to facilitate a symmetrical layout that helps maintain the electrical symmetry required for push-pull operation. Figure 1 shows the circuit diagram of the amplifier, with the parts list given in Table 1. The amplifier is a classical push-pull configuration, using a simple L-C network for impedance matching and transformer-coupling to obtain complementary gate drive signals. A wideband wire-wound transformer output circuit is used, with a conventional bifilar-wound RF choke for DC power supply isolation.

Short, low inductance interconnections are easily made using the ARF444/ARF445 devices, because they can be mounted symmetrically in a common source configuration. In particular, the gate circuit should minimize inductance to avoid instability and losses when that inductance is combined with the high capacitance of the gates. Similarly, the frequency response of the output circuitry is improved with minimum stray inductance due to interconnections [1].

The amplifier is operated directly from the PFC 300 VDC power supply, eliminating the DC-DC converter, and is constructed on a heat sink sized for proper dissipation at the expected power levels. Figure 2 shows the component placement on the PC board and heat sink. The common source design of the package allows the device mounting to be accomplished without an insulator, thus allowing good heat transfer to the heat sink with the use of thermal grease.

Input Network

The input network provides a 50 ohm impedance to the driver source and transformation of the MOSFET

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Figure 1. Schematic diagram of the 1 kW 13.56 MHz power amplifier.

gate impedance, as well as balanced drive for push-pull operation. The input network comprises capacitor C1, plus the input capacitance of the power MOSFETs and the series gate

AYDIN

resistors, both transformed by T1. The proper selection of C1 tunes the input network for minimum input return loss at maximum power output [2]. Transformer T1 provides a 9:1

Part Number	Description
R1, R2	10Ω 1W
R3-R18	4.7Ω 1W
C1	200 pF Chip Capacitors
C2-C5	0.1 µF Chip Capacitors
C6-C10	0.1 µF Disk Ceramic
C11, C12	0.01 µF Disk Ceramic
Q1, Q3	ARF444
Q2, Q4	ARF445
L1, L2	VK200-19/4B
L3, L4	0.27 μH: 6T, #18AWG,
	ID=0.438 in.
RFC1	2T, #14 PTFE insulated twisted
	pair on a Fair-Rite shield bead,
	#2643665702, μ _i = 850
T1	9:1 conventional transformer;
	3:1T, #18 stranded PTFE
	insilated wire on two Fair-
	Rite #2643540002, $\mu_i = 850$
T2	1:1 conventional transformer;
	2:2 T, #14 stranded PTFE
	insulated wire on two stacks
	of three Fair-Rite shielded
DECI	bead, #2643102002, $\mu_i = 850$
Drui	or, #16 twisted pair stranded
	stacked Indiana Concerd
	toroida #E694 10 01 195
	wroids, #roz4-19-Q1, $\mu_i = 125$

Table 1. Parts list for the 1000 W power amplifier.

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impedance transformation of the MOSFET input impedance. It is constructed using two Fair-Rite cores #2643540002, $\mu_i = 850$, with 3 turns of stranded PTFE coated #18 wire on the primary and 1 turn of stranded PTFE coated #18 wire on the secondary. The secondary is coupled through the DC blocking capacitors C2-C3 and C4-C5 and resistors R3 through R18 to the gates of the MOSFETs. The resistorinductor combinations R1-L1 and R2-L2 stabilize the push-pull amplifier at low frequency and provide the MOS-FETs with a DC ground reference to insure the gates do not float to an unwanted DC potential, thus unbalancing the amplifier bias points. The parallel resistors R3-R6, R7-R10, R11-R14 and R15-R18 are placed in series with the gates of the MOSFET to prevent high frequency oscillation, common when paralleling MOSFETs [3].

Output Circuit

The 300 VDC power input is delivered through a balanced feed choke [4]. The choke is designed to create a zero DC magnetic bias in the core when both transistors draw the same average current. With the devices operating 180 degrees out of phase, the construction of the windings presents a high impedance at 13.56 MHz to the drain of each MOSFET. The choke is constructed by winding 6 turns of #18 stranded PTFE coated twisted pair around three stacked Indiana General toroids #F624-19-Q1, $\mu_i = 125$. The output of the power devices is

The output of the power devices is coupled to the output transformer T2 through two 0.37 μ H inductors. The transformer is a wideband 1:1 conventional transformer. No output filtering was used in the test amplifier, which has the third harmonic 30 dB down and the second harmonic 55 dB below the 1000 watt output power level.

The transformer is constructed by winding 2 turns of #14 stranded PTFE coated wire for the primary and 2 turns of #14 stranded PTFE coated wire for the secondary around two stacks of three Fair-Rite #2643102002 shield beads, $\mu_i = 850$.

Performance Measurements

The test amplifier was operated under two conditions. First the amplifier was driven with a 13.56 MHz RF signal, modulated by a 1 kHz square wave, at a 50 percent duty cycle, up to a peak power out of 1200 W. Next, the amplifier was driven with a 13.56 MHz CW RF signal up to a continuous power out of 1000 W. Due to the close correlation of the modulated data and the CW data it was concluded that there is significant thermal margin when using four 300 W devices at 1000 W CW.

Figures 3 through 6 show the performance data for this amplifier. Figure 3 is a plot of P_{out} versus P_{in} and Figure 4 shows gain versus P_{out} . The curves show the classical class C characteristics, with low gain at low power output, improving as the output power increases. The gain peaks at 16.9 dB when the amplifier output is 800 W, with a roll-off to 15.9 dB at 1200 W.

Efficiency versus P_{out} is shown in Figure 5. As would be expected in



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Figure 2. Layout of the amplifier, showing placement of major components and positions of input and output transformers.

class C, the efficiency is over 50 percent at power output above 300 W. The efficiency rises to an outstanding 80.4 percent at 1000 W, continuing upward to 84.4 percent at 1200 W output. Figure 6 is total amplifier power dissipation versus P_{out} .

300 Volt Power Supply

The topology chosen for the 300 volt PFC power supply is the commonly used continuous mode boost converter. This topology is the most popular where power requirements are greater than 750 W. Figure 7 is a simplified schematic of the regulator which is implemented using an APT5012JNU2 and a Unitrode U3854 controller IC [5, 6,7].

The regulator operates by the controller sensing the rectified DC input and controlling the ON and OFF time of Q1 such that the current in L1 closely follows a sine wave which is in phase with the AC line voltage. During the OFF time of Q1 the inductor fly back transfers some of the stored energy in the inductor to the output storage capacitor. The controller senses the output voltage and adjusts the average current in the inductor such that the regulated voltage on the output capacitor is maintained at 300 V.

Conclusion

This paper has descibed a recent advance in commercial solid state RF power device and circuit technology. The high quality, low cost, components and circuits described here now make it possible to deliver solid state, 10,000 watt (or more), 13.56 MHz power supplies costing less than an equivalent



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Figure 3. Input power versus output power for the test ampliifer.



Figure 5. Efficiency versus output power.

tube-type RF power supply.

The combination of high voltage operation, high gain, and efficiency of 80 percent make this technology exciting just for performance alone. Com-



Figure 4. Amplifier gain versus output power.



Figure 6. Total amplifier power dissipation versus power output.

bine that performance with component costs that allow for multi-kilowatt, 13.56 MHz amplifiers to be built at less than \$0.25 per watt and you now have the first real breakthrough in



Figure 7. Simplified circuit diagram of the power factor correction power supply.

commercial HF, RF power technology in over a decade.

This is only the beginning. The commercial technology detailed in this paper will be evolving quickly into solid state devices and circuits for higher frequency, higher power, and even higher operating voltages.

To obtain more information on these MOSFETs, contact the author at (503) 382-8028, or circle Info/Card #251. RF

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INA-30311	DC-1000	3	6.3	3.5	13	- 2	SOT-143
INA-50311	DC-1000	5	17	3.6	19	+10	SOT-143
INA-51063	DC-2400	5	12	3.0	20.5	+ 6	SOT-363
INA-52063	DC-1600	5	30	3.5	20	+17	SOT-363
MGA-86563	500-6000	5	15	1.6	20	+15	SOT-363
MGA-87563	500-4000	3	4.5	1.6	14	+ 8	SOT-363



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RF products

Signal Simulator

Microdyne Corporation's Aerospace Telemetry Division has unveiled its new general purpose signal simulator, TSS-2000, for use in test and measurement research. The unit offers both internal and external modulation capabilities, acting as a signal simulator, signal generator and sweep generator. It provides +20 dBm maximum output power, multiple modulation formats, narrow and wide range deviation, and data rates up to 20 MHz. Sweeping capabilities are from 10 to 600 MHz (optional frequency range) and continuously in 200 MHz segments in the 1400 MHz to 2500 MHz range. Doppler simulation can reach up to 100 kHz with triangular or sawtooth patterns. Modula-

tion formats include: AM. FM. PM, PCM/FM, PCM/PM, PCM/BPSK, TV/FM (ext.). External I and Q modulation inputs are also included. When simulating a PCM data stream, the pseudo-random data is 1023 or 2047 bits, NRZ-L or Bi-Phase L and is fully compatible with major BER test sets. The TSS-2000 is phase locked to an internal reference in order to achieve the necessary frequency stability and low phase noise. An external 5 or 10 MHz reference signal can be applied to the unit to obtain even higher stability. Remote control is via IEEE-488, RS-232C, or RS-422 interface ports on the rear panel. Microdyne Corp. INFO/CARD #250



Transmitter/ Receiver Pair

RF Monolithics has introduced two new members of its Virtual Wire[™] product family. The HX2000 transmitter and companion RX2010 receiver operate at 916.5 MHz, within the 902 to 928 MHz ISM band. The HX2000 is a miniature, surface mountable, transmitter module with self-contained RF functions that shorten development time. The transmitter



employs on-off keyed modulation and is designed to be driven from a 3V CMOS logic signal. The carrier signal is quartz SAW stabilized, and a SAW filter is used to suppress output harmonics. The RX2010 receiver incorporates RFM's amplifier-sequenced hybrid (ASH) receiver architecture. The receiver supports a 10 kb/s baseband data rate and has low external parts count. North American unit pricing in 1,000piece quantities is \$8.02 for the HX2000 transmitter and \$20.84 for the RX2010 receiver. **RF** Monolithics, Inc. INFO/CARD #249

622 MHz VCXO

Raltron Electronics announces a high speed voltage controlled crystal oscillator (VCXO) for use in 622 MHz



phase locked loops for SONET and SDH data concentrators and other high frequency, wide bandwidth PLL applications. Model VH-7126 VCXOs are available in both traditional negative-going ECL outputs and also new positive-going PECL outputs. The standard center frequency is 622.08 MHz, but other frequencies in the 250 to 750 MHz range are also available. Basic frequency stability is specified at ±15 ppm maximum over the temperature range of 0 to +70 °C. Input control voltage range of 0.5 to 4.5 V yields a standard frequency control range of ±70 ppm. Output jitter is held to 50 psec pp. Pricing for the VH-7126 is less than \$80 in **OEM** quantities.

Raltron Electronics Corp. INFO/CARD #248

Amplifier Chip Set

Celeritek's CCS1933 is a twochip set designed to provide a compact, 2W, RF power amplifier for North American PCS base stations, Japanese PHS base stations, and many industrial applications in the 1.85 to 2 GHz band. The chip set operates from a 5 V power supply and consists of Celeritek's CMM1301 integrated driver amplifier and CFK2162 matched power stage. The CCS1933 delivers at least 35 dB of gain, +33 dBm minimum output power, and achievable efficiency of greater than 45 percent. Because of its high linearity, the chip set fully complies with stringent Bellcore requirements for PI/4 DQPSK modulation of minimal spectral



regrowth in adjacent channels. Production quantities of 500 are available in 30-45 days ARO and are priced at \$40.50 per chip set. **Celeritek** INFO/CARD #247

High Dynamic Range Mixer

Watkins-Johnson's HDM11 high dynamic range FET mixer is intended for cellular applica-



tions. The surface-mount mixer operates with an LO range of 800 to 1000 MHz, RF range cf 800 to 1000 MHz, and IF range of 10 to 100 MHz. Typical 3IIP is +37 dBm and nominal LO drive is +17 dBm. Typical minimum port-to-port isolation is 25 dB and 50 dB for LO-RF and LO-IF isolation, respectively Typical maximum SSB conversion loss is 7.0 dB for an IF at 10 MHz and 7.5 dB for an IF at 100 MHz. Typical 1 dB compression occurs at +23 dBm. At 5 VDC, the FET mixer typically consumes 25 mA. Watkins-Johnson Co. INFO/CARD #246

TEST EQUIPMENT

VNA Software

A new radio-measurements personality from Hewlett-Packard simplifies the user interface for HP 894000 series vector signal analyzers. The personality sets up the analyzer to automatically measure adjacent channel power, occupied bandwidth, modulation accuracy, frequency tolerance and 10-burst average error-vector magnitude on burst or continuous signals. The HP 89451A is available for \$510. Hewlett-Packard Co. INFO/CARD #245

Antenna System Tester

The Wiltron company announces the Site Master VSWR/return loss and fault location tester. Site Master is a hand-held, miniaturized, vector error-corrected reflec-



tometer that weighs only 2.2 pounds. It incorporates a synthesized source, directional bridge and "smart⁹ synchronous measurement technology that is immune to interference. The Site Master has a starting price of \$3,950.

Wiltron Co. INFO/CARD #244

Capacitance Meter

Boonton Electronics' family of capacitance meters features the ability to resolve and display minor component losses in the presence of a large reactive component in capacitors, inductors, and resistors at 1 MHz. All the meters make true three-terminal measurements that shunt stray capacitance and yield true end-to-end capacitance of the device under test. Model 7200 is microprocessor controlled and has programmable test levels, internal and external bias. Price for the Model 7200 is \$5,475. Boonton Electronics Corp. INFO/CARD #243

Spectrum Analyzer

The PA2500 spectrum analyzer from DKD Instruments turns your PC into a full featured spectrum analyzer. Consuming less than 10 W, it covers the 100 kHz to 2.4 GHz range. Spurious free dynamic range is 80 dB, and with the optional internal programmable 50 dB step attenuator, it can accurately measure signals from -135 to +20 dBm. Internal gain compensation and power calibration give power accuracy to ±2 dB. The software supports marker functions, trace math, overlays, autologging and hard copies to a printer. Price is \$6995.99. **DKD Instruments INFO/CARD #242**

Arbitrary Waveforms

Wavetek's model 296 is a 50 MHz multichannel arbitrary waveform generator with advanced waveform sequencing capability. Model 296 contains up to four independent 50 MHz channels and can link up to 4,096 waveform segments. Output signals can have 15 Vpp amplitude (80 Vpp with optional high voltage module) and 2 ppm frequency accuracy. Operation is via a mouse-controlled graphical user interface. U.S. list price is \$7,245. Wavetek Corp.

INFO/CARD #241

Antenna Tester

Bird Electronics announces the AT-800, a hand-held antenna tester for cellular and other 800-960 MHz services. The AT-800 uses a built-in RF source to measure VSWR, match efficiency, and return loss at single frequencies, or automatically sweeps over a user-specified frequency range. The display shows numeric measurements and high resolution graphic plots. Bird Electronic Corp. INFO/CARD #240

SEMICONDUCTORS

Receiver Amplifier

The MPS-0924A9-88 is a low noise high dynamic range amplifier module designed for ultra-linear applications. Paired amplifier stages in a surface mount package are externally hybrid combined to produce a balanced amplifier which has 1.5 dB noise figure and +38 dBm IP3 while consuming 1.2 W from a single positive voltage supply. Gain is 18 dB with ± 0.5 dB flatness over the operating bandwidth. **Microwave Technology**

INFO/CARD #239

Spread Spectrum IC

The S20043 direct-sequence spread-spectrum transceiver IC is highly programmable, providing users with thousands of possible programmable pseudo noise code words in lengths up to 2047 and data rates from 100 bps to 4 Mbps. The receiver and transmitter are completely independent, allowing either full-duplex or half-duplex operations. Samples are priced at \$85 each and are delivered in a 68-pin PLCC. Pricing for quantities of 10,000 or more is projected at \$23.50 each. American Microsystems, Inc. INFO/CARD #238



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INFO/CARD 45

55

RF Power MOSFET

Motorola's MRF182 and MRF183 RF power transistors offer a bottom side source that eliminates DC isolators and reduces common mode inductances. At 1 GHz, the MRF182 delivers 30 W P_{out} , 13 dB gain, and 55 percent efficiency; the MRF183 delivers 45 W P_{out} , 12 dB gain, and 55 percent efficiency. Price in low volumes is \$93.00 for the MRF182 and \$108.50 for the MRF183. Motorola Semiconductor INFO/CARD #237

Linear, 100 W MOSFET

California Eastern Labs introduces a 100 W power MOSFET for Band IV and V TV linear transmitters. Designed for broadcast transmitters in the 470 to 860 MHz band, NEC's new 30 V, class AB push-pull NEM0899F01-30 Si MOSFET delivers high output power, high gain and high efficiency



under a variety of drive conditions. At 860 MHz, V_{DD} = 30 V, and I_{dg} = 300 mA, the MOSFET typically produces 100 W with 12 dB gain and 50 percent drain efficiency. California Eastern Laboratories INFO/CARD #236

Micro Diodes

M-pulse Microwave's family of Micro SMT[™] diodes includes PINs, Schottkys, and mixer-ring-quad families. The diodes are packaged using Micro SMT technology, which allows devices to be packaged while still in wafer form. The devices have a package inductance in the range of 0.1 to 0.2 nH and a package capacitance in the range of 0.02 to 0.03 pF. Micro SMT is a trademark of ChipScale, Inc. **M-pulse Microwave**

M-pulse Microwave INFO/CARD #235

PHEMTs

Stanford Microdevices has announced a line of pseudomorphic high electron mobility transistors (PHEMTs) which achieve up to 50 percent power added efficiency from 500 MHz to 26 GHz. At 2 GHz these FETs have 16 dB of gain with 0.25 noise figure. The SPF-2298 has typical output power of +24 dBm at 1 dB compression when biased at +5 V and 100 mA. Typical IP3 is +33 dBm. Stanford Microdevices INFO/CARD #234

SUBSYSTEMS

Upconverter

Mu-Del model MUCM-10 is a multi-mod-

ule, independently removable five channel upconverter unit. The modules are fully enclosed and isolated from each other. Input frequency of the main chassis is 10 MHz ± 3 , output frequency is 1435.5 to 1535.5 MHz, tunable in 1 MHz step size at the front panel of each module. Image rejection is at least 60 dB below output and spurious response is -60 dB.

Mu-Del Electronics, Inc. INFO/CARD #233

Telephone Interface Unit

Stanford Telecom announces the release of the STel model 2700 telephone interface unit (TIU), providing the interface between the single channel per carrier VSAT equipment and external telephone equipment. The voice compression algorithm used is compatible with the present ITU G. 728 standard 16 kbps and the future G .279 for 8 kbps. The TIU can switch between 19.2 and 9.6 kbps and can operate at multiple data rates. Stanford Telecommunications, Inc. INFO/CARD #232

GPS Patch Antenna

Toko America has introduced the DAK series of miniature dielectric ceramic antenna elements for use in Global Positioning Systems (GPS). The rectangular micro-strip design is intended for GPS C/A



right-hand circular polarization wave reception. Its 25 mm² surface and 4mm height makes this product approximately one quarter the size of a traditional antenna element without sacrificing sensitivity. **Toko America, Inc. INFO/CARD #231**

HF Receiver/Translator

Interad Ltd. introduces model 9450, an eight-channel, wideband HF receiver with input frequency range from 0.5 to 32 MHz and output range from 1.0 to 11 MHz. The unit has eight channels – one independent and seven others sharing a common LO. Receiver bandwidth is 10 MHz and nominal gain is 53 dB. Synthesizer tuning speed is better than 1 ms and synthesizer step size is 500 kHz. Minimum output IP3 is +44 dBm. Interad Ltd.

INFO/CARD #230

Airborne Transmitter

Aydin Vector's T-300 S/L series subminiature airborne UHF, video/telemetry transmitters are available in 2, 5 and 10 W power output. The transmitters measure $1.50 \times 2.50 \times 0.75$ inches and weigh less than 4 oz. The transmitter complies with IRIG-106-93 and MIL-STD-461 EMI requirements. Aydin Vector Division INFO/CARD #229

SIGNAL SOURCES

Phase Locked Source

Communication Techniques has introduced a low cost, low phase noise, high performance, phase locked coaxial resonator oscillator available from 750 MHz to 3000 MHz. Typical phase noise for an 860 MHz unit is -108 dBc at 1 kHz offset, -115 dBc at 10 kHz offset, and -130 dBc at 100 kHz offset. Spurious levels are typically -100 dBc. Output power is normally +13 dBm. Communication Techniques, Inc. INFO/CARD #228

Ultra-Stable OCXO

MTI - Milliren Technologies, Inc. introduces their next generation of ultra high stability / high reliability oven-controlled crystal oscillators. The 260-0536 (10 MHz) utilizes an SC-cut resonator to offer thermal stability of $\pm 1.0 \times 10^{-9}$ from -30 to +70°C. Aging is specified at 3.0×10^{-10} per day (5.0×10^{-8} per year). Phase noise is -125dBc/Hz at 10 Hz offset, with a noise floor cf -160 dBc/Hz. The device measures 2.0×2.0 × 1.5 inches and is priced at \$480.00 each in quantities less than 100. MTI - Milliren Technologies, Inc.

MTI - Milliren Technologies, Inc. INFO/CARD #227

Miniature OCVCXO

Oak Frequency Control Group's 4598S OCVCXO, available from 10 to 25 MHz, features a package outline of $38.0 \times 26.5 \times$ 15.0 mm. The 4598S meets a temperature stability spec of $\pm 5 \times 10^{-9}$ over 0 to 70 °C and features aging of ± 0.1 ppm per year. The OCVCXO operates from a +5 V supply. Typical pricing with standard options is \$165 each in 1000-piece quantities. Oak Frequency Control Group INFO/CARD #226

Miniature OCXO

Reeves-Hoffman has introduced the Model 105 miniature OCXO. Housed in a standard $1.5 \times 1.5 \times 0.53$ inch TCXO package, the Model 105 offers high stability for small size, rack mounted or portable applications. The 105 is able to drive TTL and CMOS loads for more design flexibility. A variety of temperature and stability options are available. **Reeves-Hoffman**

INFO/CARD #225

Low Phase Noise Oscillator

Model 2930201 from Piezo Crystal utilizes Piezo's SC-cut crystals. The frequency range is from 5 to 12 MHz. Typical phase noise at 10 MHz is -110 dBc/Hz at 10 Hz offset. The aging rate at shipment is 5×10^{-10} /day. Frequency stability is $\pm 1 \times 10^{-8}$ from -20 to +60 °C. Size is 2.00 × 2.00 × 0.75 inches, and price is \$190 each in quantities of 500. **Piezo Crystal Co. INFO/CARD #224**

TCXOs

Vectron Laboratories' series of PC board mount, temperature compensated crystal oscillators are available in frequencies from 500 kHz to 75 MHz. Models CO-511 and CO-557 provide aging rates of less than $1 \times$ 10^{-6} /year and temperature stabilities ranging from $\pm 5 \times 10^{-7}$ from 0 to 50 °C and $\pm 2 \times$ 10^{-6} from -55 to +85 °C. The CO-557 series measures $1.4 \times 1.06 \times 0.50$ inches, and the CO-511 series measures $1 \times 1 \times 0.50$ inches, with an alternate European CO-15 package. Vectron Laboratories, Inc. INFO/CARD #223

ocxo

Frequency Electronics' model FE-101 is a rugged, compact, ultra-stable subminiature crystal oscillator with temperature stability of 1×10^{-8} from -55 to +85 °C. The OCXO warms up to stabilized frequency in less than two minutes and has g sensitivity of $3 \times 10^{-10}/g$. Steady state power consumption is 1.75 W at 25 °C. Model FE-101A measures $1.27 \times 1.33 \times 1.33$ inches. Frequency Electronics, Inc. INFO/CARD #222

DISCRETE COMPONENTS

SMT Porcelain Capacitors

North American Capacitor Company's MPR Series of micro-porcelain multilayer capacitors operate at microwave frequencies up to 30 GHz. Proprietary porcelain materials enable typical minimum Q factors of 10,000 at 1 MHz and 25 °C. The MPR Series capacitors are available with capacitances ranging from 0.2 pF to 0.1 μ F and are available in chip and pellet configurations; each in both 1.4 × 1.4 × 1.45 mm and 2.79 × 2.79 × 2.59 mm case sizes. North American Capacitor Co. INFO/CARD #221

Expanded Trimmer Lines

Voltronics has added higher capacitance values to its J lines of ceramic chip trim-



mers. The JZ line now has a 40 pF part, the JZ400, in addition to its 3.0 through 30 pF



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max. ranges, and the smaller JR line now has 30 and 40 pF parts in addition to its 3.0 through 20 pF max. ranges. Prices are well under \$1.00 each.

Voltronics International Corp. INFO/CARD #220

SIGNAL PROCESSING COMPONENTS

Attenuator

Mini-Circuits has introduced a low cost, surface mount fixed attenuator with a very wide DC to 7 GHz bandwidth. The PAT-1 is a miniature $0.21 \times 0.21 \times 0.053$ inch, 50 ohm unit housed in a ceramic package and exhibits excellent input/output matching throughout the entire frequency range with a maximum VSWR at 1.3:1 at midband. The device offers a 1 W rating at 25 °C case temperature. This attenuator is priced at \$2.95 each in quantities of 10 to 49. Mini-Circuits

INFO/CARD #219

High Isolation Mixer

MITEQ's DM0052HA2 and DM0052LA mixers are constructed using a new microwave balun (patent pending) operating from 0.5 to 2.0 GHz with an IF response from DC to 500 MHz. This design produces unusually high port-to-port isolation and the "h" version performs as an up- or down converter covering most PCN and communication applications requiring high input signal levels. Both designs can also be used as biphase modulators or phase detectors with low DC offset voltages. MITEQ

INFO/CARD #218

Delay Lines

MICRO-COAX has introduced a family of compact custom delay lines. Standard delay times range from 1 to 200 ns with insertion loss ranging from 1.2 to 5.9 dB at 900 MHz. Dimensions of standard models range from 0.75 inch high × 1 inch diameter to 2.25 inch high × 2.75 inch diameter. Each delay line is engineered to the specific requirements of a customer's application. MICRO-COAX INFO/CARD #217

1 GHz+ SAW Filter

Three patents are pending on an RF SAW filter designed by Murata Electronics. Murata's SAW filter is based on zinc oxide printed on a sapphire substrate and delivers high performance, even above 1 GHz. This new design provides a larger electromechanical coupling coefficient, higher propagation velocity and smaller wave propagation losses. Other design enhancements include a 50 ohm termination so that no external adjustment circuit is required. Pricing is approximately \$3 to \$4 each, depending on volume. Murata Electronics North America INFO/CARD #216

Lowpass Filters

RLC Electronics introduces its new line of lowpass filters with spurious-free operation up to 40 GHz. These units are designed



using a low-ripple Chebychev approach and offer excellent VSWR and rejection parameters, while maintaining an extremely small size. Prices start at \$150.00 in unit qty. **RLC Electronics, Inc. INFO/CARD #215**

IF SAW Filters

The SWS Series SAW filters from Toko America are multimode resonator filters that feature narrow bandwidths of 30 kHz and insertion losses less than 5 dB. The use of temperature stable ST-quartz material allows for a broad operating temperature range of -30 to +80 °C. The series is available in six standard center frequencies: 83.16, 85.05, 86.85, 86.01, 90.0 and 130.0 MHz. Pricing in 100 piece quantities ranges from \$15 to \$20. Toko America, Inc. INFO/CARD #214

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RF tutorial

Test Setups for Measuring Intermodulation Distortion

By Gary A. Breed Editor

One of the fundamental performance measurements for RF circuits is intermodulation distortion (IMD). This test procedure and its results define the linearity of amplifiers and the performance of receiving systems in the presence of multiple signals. This article presents the typical test configurations for IMD testing, with some additional notes on test procedures and interpretation of results.

Intermodulation distortion, as its name implies, is the presence of unwanted signals that have been created by mixing action (modulation) among signals in circuits that are not ideally linear. The term mixing is exactly that same as is used for frequency conversion, since IMD products are defined in that manner:

$IMD_x = n f_1 \pm m f_2$

that is, a specific IMD product is the mixing product of a fundamental or harmonic of one one signal and a fundamental or harmonic of another signal. The expression is not resricted to two signals; it can be expanded to any number of individual signals which can create IMD.

From the above equation, it follows that IMD measurements require at least two signal sources, f_1 and f_2 , along with some kind of detector that can observe the frequencies where the various IMD products are expected to appear. To determine where those frequencies will be, we need to know the expected range of n and m.

The order of the IMD product is defined as n + m. Therefore, a secondorder IMD product can be either the sum or the difference of two frequencies. Third-order products are twice one frequency, plus and minus the other frequency, giving four possible IMD products. Without working out all the math, odd-order IMD products occur at intervals equal to the differ-



Figure 1. Relationships of third-order IMD products to the fundamental frequencies that caused them.

ence in frequency between f_1 and f_2 . If those two frequencies are close together, the odd-order IMD products will be very close to the two fundamental frequencies, distributed in a distinctive pattern (Figure 1).

The most common types of IMD testing use this characteristic to advantage. First, the IMD products appear in the same receiver or transmitter tuning range as the fundamentals. This mimics the real world; in a receiver, two strong signals just outside a the IF filter passband may cause IMD that is detectable within the passband. In a transmitter, IMD generated within the transmitter, or involving other nearby transmitters, may create distortion products that are so close to the desired signal that they can not be filtered out, corrupting the transmitted signal.

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much less practical interest, since most radio systems include filtering that reduces potentially harmful IMD to insignificant levels. However, there are still plenty of systems with broadband front-ends and wideband amplification that may benefit from measurement of widely-separated IMD products. As a general rule, though, acceptable close-in IMD performance also means acceptable far-removed IMD performance, and is much easier to measure.

Test System Architecture

There are two basic test setups used for third order IMD measurements. The first and most common, shown in Figure 2, is for testing individual circuits, and consists of two signal sources, a combiner, the necessary interconnections to the device under test, and a receiver or spectrum analyzer to detect and measure the distortion products.

Although the arrangement is very straightforward, there are several important considerations that must be followed. First, the signal sources must be stable and accurate in frequency, with very low noise to avoid ambiguity when measuring very low levels of IMD. Also, the signal sources must be closely matched in amplitude to avoid variations due to the test setup. Unequal amplitude sources will create unequal amplitude distortion products. We want to measure the effects of the circuit under test rather than the characteristics of the test instrumentation!

Such test systems often include an attenuator between the combiner output and the device under test input. This allows the engineer to precisely balance the amplitudes of the signal generators at a fixed level, then separately adjust the input to the test circuit. This extra attenuator is unnecessary with a well-designed combiner and high quality signal generators.

Also, the receiver or spectrum analyzer must not contribute errors to the test results. Of particular concern is avoiding signal levels that may overload the input circuits of these instruments, creating a new set of distortion products that can confuse or even obscure the desired measurement. A typical test to see if internal distortion is a problem is to attenuate the input to the receiver or analyzer by 10 dB, and make sure that the measured results also change by exactly 10 dB.



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Figure 3. Test setup for receiver IMD testing, using the receiver as part of the test system, resulting an an overall performance measurement.

If not, further investigation is necessary to establish the proper signal level, or to locate the source of the problem if signal levels are within the instrument's specifications.

The second test setup is specifically for testing of receivers. The receiver becomes part of the test system, as shown in Figure 3. In this setup, f_1 and f_2 are again supplied by two signal generators through a combiner. Because receivers operate with very low level inputs, the attenuator mentioned earlier is used by most engineers for more precise control over test signal levels. The output of the receiver (audio or baseband) is measured using an AC voltmeter.

Test Procedures

Measurement procedures are similar for different types of circuits, but because the range of expected results can vary widely, there are some test procedure variations, as well. We'll use two examples to illustrate the process: a medium-power amplifier and a receiver.

The most common test for power amplifier linearity is a two-tone test with the test signals separated by 1 or 2 kHz. This represents the "real world" where modulation creates a composite signal with numerous frequency components, but within a normal passband that is rarely less than 2 kHz. The IMD products observed from this test would correspond to spurious signals generated by IMD among the components of the modulated signal. By establishing a standard test of 2 kHz spacing (or another representative spacing), a repeatable test can be performed, and meaningful comparisons of a "before and after" nature can be made, as well as comparisons of different amplifiers.

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The two test signals are set to the desired amplitude to drive the amplifer under test. This amplitude may be varied to examine amplifier performance at several power levels. This can be especially important for determining the power level at which the IMD passes the threshold of acceptable performance. (The threshold may be anywhere from 20 dB below carrier to 50 dB below carrier, depending on the application).

This test is almost always run with a spectrum analyzer as the detector. The frequency span of the analyzer is set to observe the two test signals along with a number of odd-order IMD products. Thus, a complete picture of the amplifier output can be observed at once.

A receiver is often tested as a complete unit, when the overall input-toouput performance must be known. In this case, the test signals are set at a frequency separation that avoids any ambiguity due to receiver design, maintained for the same before-andafter and unit-to-unit comparisons noted above for amplifier testing.

The signal separation should be small enough that the test signals and the IMD products fall within the frontend passband of the receiver. A receiver with a front-end preselector will require a closer spacing of test frequencies than a wideband receiver. Typical test signal spacings are 20 kHz, 100 kHz and 1 MHz.

The signals must be spaced far enough apart so that the IF bandwidth of the receiver effectively attenuates the stronger signals when the IMD products are measured. For example, if 20 kHz spacing is used, the attenuation of the IF filter at 20 kHz from the center frequency must be much more than the amplitude difference between the test signals and the IMD products.

Once the test signals are applied to the receiver input, the baseband or audio output is monitored. A reference is set at the level of the received test signals, then the receiver is tuned to the frequency of the expected IMD products. The difference in amplitude is readily measured. Of course, all gain control functions must be disabled to avoid erroneous results.

Reference Levels

When comparing published measurement data, we must remember that there are two methods used for IMD specifications. One is to use the amplitude of each test signal as the reference point. In this case, the IMD will be specified as "x dB below either of the test signals."

The other common reference uses the peak amplitude of the composite two-tone test signal, which is 6 dB higher than either test signal. On a spectrum analyzer display, the attenuation will be set so that the test signals are displayed 6 dB below a reference line.

Both reference conventions are valid, but to make comparisons, we must remember to determine which one was used. Correlation is simple; the difference between the results is always 6 dB, with the peak amplitude measurement showing 6 dB better IMD performance than the equivalent individual test-tone referenced measurement.

Conclusion

This simple introduction to IMD testing is only a beginning, intended to outline equipment and methods used in IMD testing. In particular, testing with more than two tones is growing in importance, with the growth of cellular and PCS systems which have multiple channels amplified in a single transmitter, or captured in a single receiver. *RF*

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FEST & DESIGN

FEATURES

Prediction of Conducted Emissions in Switched-Mode Power Supplies 10 Gregory Kyriazis

Switched-mode power supplies are a challenge for EMC engineers. The author describes his work in developing SPICE models to help predict emissions from this type of equipment.

Power Transistor Inductive Load EMI Control 14

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Power MOSFETs are commonly used to switch relays and solenoids. The inductive "kick" generated by collapsing magnetic fields can generate significant EMI. This article describes methods for reducing this EMI using a gate capacitor and a snubber circuit.

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18

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Gary A. Breed

The CE mark will soon be required on all electrical and electronic products sold in the European Union. Among the specified performance standards are EMC requirements. This note covers the methods that manufacturers may use to assure compliance and obtain the CE mark.

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*Info/Cards can be found on page 130 of the accompanying issue of *RF Design*.

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News

Reverberation and Anechoic Chamber Operators Meeting

The Naval Surface Warfare Center in Dahlgren, VA is sponsoring the 1995 Reverberation Chamber & Anechoic Chamber Operators Group Meeting. The meeting will be held December 5-7, 1995 in Dahlgren. Topics will include military test applications, test standards, industrial and commercial testing, new test technologies, automotive testing, medical/biological testing, and others. For more information, contact: Naval Surface Warfare Center, Dahlgren Division, Attn: Michael O. Hatfield/Code F-52, 17320 Dahlgren Road, Dahlgren, VA 22448; email: MHATFIE@RELAY.NSWC.NAVY.MIL

Lindgren and Monsanto in Distributor Agreement

Lindgren RF Enclosures and the Metallized Materials Group of Monsanto Company have concluded an agreement making Lindgren the exclusive U.S. and Canadian distributor for Flectron metallized materials for architectural shielding products. Flectron materials use polyester nonwoven fabric coated with either copper or nickel-on-copper, and are available as 54 inch wide roll goods, and in roll tape form.

DoD Renews IITRI EMC Support Contract

IIT Research Institute announces that its contract to provide support to the Department of Defense in Annapolis, Maryland has been renewed for a minimum period of 39 months. The contract to provide technical support to the DoD Joint Spectrum Center (JSC) is for a maximum of \$119 million, with an option for an additional two years. IITRI's JSC Support Group helps to guarantee the electromagnetic compatibility of military communications and electronic weapons systems. Its engineers are frequency called on to

solve spectrum management and electromagnetic interference problems involving the military services, the DoD, or the civil sector. IITRI has managed the JSC Support Group (formerly known as the Electromagnetic Compatibility Analysis Center Support Group) for more than 30 years. IITRI is headquartered in Chicago and is affiliated with Illinois Institute of Technology.

D.L.S. Opens New Facility With 7 EMC Test Labs

On July 5, D.L.S. Electronic Systems opened its new 16,000 square foot EMC test facility in Wheeling, IL, with (2) FCC/CISPR pre-scan semi-anechoic chambers; (2) IEC 801-2 & 4 test rooms; (2) IEC 801-3 test rooms, including a 24×35 ft. semi-anechoic room capable of testing at 20 V/m at 3 meters; and (1) IEC 801-5, 6, 8, 11, 555-2 & 3 test room. D.L.S. continues to operate its two open field test sites in Genoa City, WI.

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Last year, ANTENNA RESEARCH introduced two new product lines to the EMC community: A full range of GTEM cells for emission and susceptibility testing and Shielded Fiber Optic Links and Camera Systems for EMC testing in high electromagnetic field environments.



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News

ESCO Subsidiaries Form EMC Test Systems Group

Rantec Microwave & Electronics, Inc. and the Electro-Mechanics Company (EMCO) have formed EMC Test Systems Group, a new business unit combining the product lines of Rantec Anechoic Systems, Rantec's Ray Proof North America and EMCO. The EMC Test Systems Group is headquartered in Austin, TX.

Listings Sought for NIST Product Certification Directory

NIST's Standards Code and Information Program has awarded a contract to The Marley Organization Inc. to revise and update NIST Special Publication 774, Directory of U.S. Private Sector Product Certifications Programs. the new directory will provide data on national, regional and local systems for certifying goods for sale. Information under each listing will include name and purpose of the certifying organization, types of products certified, steps involved in the certification scheme and a pictorial index of certification marks. Organizations wishing to be listed, or interested parties who can identify qualifying organizations should contact Charles W. Hyer, The Marley Organization Inc., 412 Main St., No. 3, Ridgefield, CT 06877; tel: (203) 438-3801; fax: (203) 438-2313. Expected publication of the updated SP774 is early 1996.

ESD Association to Update Mil-Std-1686

The ESD Association and its Standards Committee have accepted an invitation from the U.S. Department of Defense to update Mil-Std-1686, Electrostatic Discharge Control Program for Protection of Electrical and Electronic Parts, Assemblies and Equipment (Excluding Electrically Initiated Explosive Devices). Originally produced by the military in 1980, the standard established the requirements for an ESD control program, and now is in its third revision. The update would become an ANSI standard and would be adopted by the military.

ANSI Publishes Report on Progress in Voluntary Immunity Standards

In a December 1994 report, ANSI committee C63 states that immunity efforts are having an increased effect on the ability of home entertainment electronics (mainly TVs and VCRs) to reject interference. As older equipment is replaced by new models that have incorporated improved designs, the number of interference complaints has continued to drop. The report also includes notes on design recommendations that would further improve immunity performance of these products.

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9

Prediction Of Conducted Emissions In Switched-Mode Power Supplies

By Gregory A. Kyriazis Inmetro



Gregory A. Kyriazis received his BSc degree in Electrical Engineering from the Universidade Federal do Rio de Janeiro in 1982 and his MSc degree in Electrical Engineering from Centro Federal de Educacao Tecnologica do Rio de Janeiro in 1995. His experience in engineering in-cludes over 10 years as design engineer and test engineer. He can be reached at Rua Republica do Peru, 136/701, 22021-040 Rio de Janeiro. Brazil; Fax: +55 21 679 1507.

Switched-mode power supplies (SMPS) create range of frequencies. Therefore it is important to predict the emission level of the equipment during the early design stage to optimize the filtering design and reduce the time to market.

The modeling of the disturbance sources in SMPS is done in the frequency domain. To convert the time domain switching waveforms into the frequency domain, the Fourier series of the waveforms are calculated. The model proposed in [1], although based on a buck converter, was used in the modelling of a flyback-type SMPS. This model is based on the equivalent disturbance generator applied to the switching transistors. The parameters used by this model were measured on a commercial SMPS sample. A SPICE simulator and a spreadsheet were used to predict the emission behavior of this SMPS.

It was evident that the model can predict the actual circuit behavior. A rationale is given for the differences between measured and calculated results.

Disturbance Voltage Types

There are basically two types of disturbance voltage present on a power bus [1]: differential mode (DM) and common mode (CM). DM disturbance voltage (V_{DM}) occurs between the leads of the intentional current path (phase- neutral or phase-phase). CM disturbance voltage (V_{CM}) occurs when the disturbance source is between ground and the phases, including neutral. The phase-ground (V_p) and neutral-ground (V_N) disturbance voltages are measured with a spectrum analyser (or EMI receiver) and a line impedance stabilization network (LISN) are: [3].

$$\begin{vmatrix} \hat{\mathbf{V}}_{\mathbf{P}} \end{vmatrix} = \begin{vmatrix} \hat{\mathbf{V}}_{\mathbf{CM}} + \hat{\mathbf{V}}_{\mathbf{DM}} \end{vmatrix}$$
$$\begin{vmatrix} \hat{\mathbf{V}}_{\mathbf{N}} \end{vmatrix} = \begin{vmatrix} \hat{\mathbf{V}}_{\mathbf{CM}} - \hat{\mathbf{V}}_{\mathbf{DM}} \end{vmatrix}$$
(1)

Modeling CM Emissions

The CM current path on a simplified schematic of SMPS is shown in Figure 1 (resistance values are in ohms). R1 and R4 are the equivalent LISN high frequency impedance. R3 and R5 are the diode bridge series resistance when forward biased. C2, R2 and L2 are respectively, the capacitance, the ESR and the ESL of the input rip-



Figure 1. SMPS CM emission model.



Figure 2. Switching transistor drain-source voltage waveform.

ple filter capacitor. V1 is the switched voltage waveform, and C1 is the parasitic capacitance to ground. This model assumes that the output filter inductor, reflected through the output transformer, is very much greater than L2, and therefore the current flows through the impedance of the input ripple filter capacitor [1]. This assumption is valid for the buck converter.

The measured values were taken from a flyback-type SMPS commercial sample without any EMI control measures. The voltage source V1 was measured with an oscilloscope (HP 1740A). C1, C2 and R2 were measured with an LCR meter (HP 4262A). L2 was estimated from manufacturer information. The values of R3 and R5 were taken from [1]. Special care was devoted to the guarding techniques used in the measurement of C1.

The switching-transistor drain-source voltage (V_{DS}) waveform was measured and approximated by a trapezoidal waveform (Figure 2), where A'' (= 400 V) is the amplitude, T_0' (= 12.4 µs) is the switching transistor cutoff time, t_{r}' (= 130

Conducted Emissions

ns) and t_{f} (= 60 ns) are respectively the rise and fall times, and T is the period. The amplitude and phase of the Fourier expansion coefficients for the one-sided spectrum of this waveform were calculated using standard techniques [3].

In the SMPS sample tested, the parasitic capacitance to ground, C_n (= C1), was mainly due to the distributed capacitance between the primary and secondary windings of the output transformer (because the switchingtransistor heatsink was well isolated from the chassis, its contribution to the parasitic capacitance was negligible). The current that flows in each elementary capacitance of the winding depends on the voltage level at each element. The potential, distance x along the winding, is $(x/l)^2 V_{DS}$. The total current is obtained integrating the effects of all the elements for the entire winding, i.e.,

$$I = \frac{jn\omega_0 C_P V_{DS}}{l} \int_0^l \frac{x^2}{l^2} dx$$

= $jn\omega_0 C_P \frac{V_{DS}}{3}$ (2)

where ω_0 is the switching fundamental frequency and n is the harmonic number. The total current flows as if the capacitance C_p were connected to a voltage source of $V_{DS}/3$. Thus, in this case study, the value of A^{''} to be inserted in the Fourier expansion of V_{DS} is one third of the measured value of the drain-source voltage waveform amplitude. This is a simplified approach; it assumes the windings are perfectly uniform, the secondary windings can be approximated by a conductive plane and the series capacitance down the winding is negligible.

The CM emission component (the voltage drop on R1 and R4 of Figure 1) was calculated using the PSPICE 5.0 circuit simulator (Microsim Co.). As this simulator gives only the first nine Fourier expansion coefficients, the circuit of Figure 1 was simulated with an AC analysis ranging from the third harmonic (192 kHz) to the 461th harmonic (29,504 MHz), assuming a voltage source with unity amplitude and null phase. Using the principle of linearity, the simulation results were then multiplied by the Fourier expansion coefficients of $V_{\rm DS}$ for each harmonic number to yield the predicted CM disturbance voltage (Figure 3).

Modelling DM Emissions

The DM current path on a simplified schematic of SMPS is shown in Figure







Figure 4. SMPS DM emission model.

4, where I1 is the current waveform through the switching transistor. The current source I1 was measured with an oscilloscope (HP 1740A). The other components are similar to those of the CM model. This model addresses only the low impedance component of DM emissions [2].

The switching transistor current waveform, $I_{DS}(t)$, was measured and approximated by the addition of two triangular waveforms, $I_{DS1}(t)$ and $I_{DS2}(t)$, as illustrated in Figure 5, where A (= 1.79 A), t_r (= 3.1 µs) and t_f (= 100 ns) are respectively the amplitude, the rise and fall times of the $I_{DS1}(t)$ current component, T_0 (= T – $T_0' = t_r + t_f$) is the switching transistor saturation time, A' (= 2.86 A) is the amplitude of the $I_{DS2}(t)$ current component, and T1 (= $t_f' = 60$ ns) is equal to the fall time of the drain-source voltage waveform. The amplitude and phase of the Fourier expansion coefficients for the one-sided spectrum of both $I_{DS1}(t)$ and $I_{DS2}(t)$ were calculated using standard techniques [3].

The DM emission component (the voltage drop on R1 and R4 of Figure 4) was calculated as described for the CM emission component, except that the simulation results from the analysis of the DM model were multiplied by the Fourier expansion coefficients of I_{DS} , for each harmonic number (Figure 6). Substituting the predicted CM and DM disturbance voltages in equation 1, for each harmonic number, gives the predicted conducted emission level (Figure 7).



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Figure 5. Switching transistor current waveform.

Shielded Output Transformer

A way of reducing primary to secondary capacitance is to provide an interwinding electrostatic shield connected to the DC supply line of the flyback converter [4]. The CM model (Figure 8) is based on the electrostatic shielding model proposed in [5] where C18 and C19 are the primary-to-shield and secondary-to-shield capacitances; C20 and C21 represent the leakage current that flows out of the shield due to the transformer and the circuit layout, respectively. These parasitic capacitances were measured using guarding techniques. The DM model is the same as presented above (tests from 100 Hz to 1 MHz indicate the shield has little or no effect for DM currents [6]). Figure 9 shows the predicted conducted emission after shielded output transformer insertion.

Experimental Validation

The measurement of the disturbance levels was carried out with a CISPR setup [7]. A computer controlled spectrum analyzer (HP330/HP8567A) was used for EMI measure-

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Figure 6. Predicted DM emission level.



Figure 7. Predicted conducted emission level.



Figure 8. SMPS with shielded output transformer, CM emission model.

ment. A peak detector was used for all the tests, since quasi-peak is not available for this model. As the analyzer displays the RMS value of the sinusoidal harmonic, 3 dB was subtracted from the calculated peak values. A line impedance stabilization network (LISN - EMCO 3825/2) was used to supply the SMPS during the measurement. The author built the differential mode rejection network (DMRN) proposed in [2], and used it to measure the CM component of the conducted emission.

The measured CM emission level of the SMPS under test is shown in Figure 10. Part of the difference between the measured and predicted CM values (Figure 3) is explained by the insertion loss of the DMRN (≈ 4 dB). An-



Figure 10. Measured CM emission level.

other reason for the difference in the low frequencies (150 kHz - 450 kHz) is that in this range the LISN presents a lower impedance value than the assumed 50 ohms. The measured conducted emission level is illustrated in Figure 11. The effect of the shielded output transformer on the measured conducted emission level is reported in Figure 12. The predicted results (Figures 7 and 9) agree fairly well with the respective measured ones.

Although originally derived for the buck converter, the equivalent disturbance generator model proposed in [1] allows an effective prediction of the flyback-type switched-mode power supply conducted emission level.

The unexplained difference between the measured and calculated values



Figure 11. Measured conducted emission level.



Figure 9. Predicted conducted emission level with shielded output transformer.

points to the development of a model that could address the high impedance differential mode emission of a flyback converter.

Ackowledgements

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Figure 12. Measured conducted emission with shielded transformer.



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Both authors can be reached at Motorola, Phoenix Technology Center, 7755 S. Research Dr., Suite. 110, Tempe, AZ 85284. Tel: (602) 413-2537, or (602) 413-2518. Controlling an inductive load such as a DC relay or low speed solenoid with a power transistor driven from a microcontroller or digital logic would seem fairly straightforward. A power transistor is selected to satisfy a few essential requirements: maximum voltage rating above supply voltage, current rating above solenoid's operating current level, a low on-voltage to keep power dissipation down (so no heatsink is required) and the ability to be driven from 5 volt logic. The solenoid's inductive "kickback" voltage is contained with an avalanche-rated power FET. Unfortunately, this design will also

By Richard Valentine and Tom Huettl Motorola Semiconductor Products Sector

Load EMI Control

Power Transistor Inductive

generate significant EMI. There are two conditions in this switching circuit that contribute to EMI: the logic signal's high speed transitions which drive the power FET, and the inductive "kickback" voltage clamp's behavior. Figure 1 shows a relay control circuit to test various EMI reduction methods. The results are shown in Figure 2(a) for the previous straightforward design. Adding a free wheeling diode across the solenoid stops the power FET from avalanching, but does not elimi-

nate EMI as shown in Figure 2(b).

Slowing the switching edges of the logic signal driving the power FET's gate will help minimize EMI because the power FET's switching times are no longer in the RF range. Logic signals usually exhibit switching edges of less than 1µs. If the power FET is switched at anywhere near this speed, serious EMI will result. One simple method to slow down the logic driving signal's edges is to add a series resistor and a gate-to-source capacitor. To minimize the chance of parasitic RF oscillations during switching the series resistor value should be 1kohm or less and the gate to source be fairly large, 0.01 to



Figure 1. Inductive load control test circuit.

1.0 μ F, in order to slow the gate drive signal transition times. The gate drive source lines must be connected close to the source, and placed out of the source to common load current path. Figure 2(c) shows the effect of just adding



Figure 2(a). Drain voltage, V_d, avalanches power FET and contributes to EMI.



capacitor value should Figure 2(b). A free wheeling diode stops power FET from avalanching, but be fairly large, 0.01 to does not stop EMI.

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Inductive Load EMI Control



Figure 2(c). Adding a 0.1 μ F gate capacitor slows down the FET and lowers EMI.



Figure 2(d).Adding a free wheeling diode along with the gate capacitor increases EMI levels.

a 0.1 µF gate capacitor which reduces EMI by slowing down the power FET's switching speed. Figure 2(d) is the same except the free wheeling diode across the load has been added. The gate RC network is a low cost fix, but does introduce a timing delay, and extra power dissipation in the power FET. The extra power dissipation occurs because of the power FET's slow turn off. The extra power dissipation may require a larger FET. Graph 1 shows the delay effect for different gate capacitor values. Generally a 50 to 100 µs delay time should not effect the application since the operating frequency for relays or solenoids is usually less than 10 Hertz.

One other point about the gate voltage switching behaviour is that power FETs exhibit high transconductance, which means it only takes a small gate voltage variation to turn the load on or off. The gate voltage variation can be determined by dividing the load current by the FET's forward transconductance. For example, an MTP3055EL's forward transconductance (g_{FS}) is 5.0 mhos minimum. If the load current is 0.2 amperes, then



Inductive Load EMI Control



Figure 2(e). Adding a 1 μ F 10 Ω snubber along with a 0.1 μ F gate capacitor minimizes EMI.

the ΔV_{gs} is only 0.04 volts. ($\Delta V_{gs} = 0.2/5$). Therefore only a small portion of the gate's voltage transition time affects the switching times of the load. This is why a large gate-to-source capacitor has to be used to slow down the gate voltage transition time.

The other EMI source is from the inductive "kickback" voltage clamp. When this device (either a free wheeling diode or zener) is activated, it generates EMI. The free wheeling diode also slows down the solenoid's or relay's mechanical turn-off performance. Replacing the free wheeling diode with a RC snubber can reduce EMI and still allow good turn-off mechanical response. The snubber capacitor value should be large enough to prevent the power FET from avalanching. The exact value of the RC snubber is determined by the specific application. A 0.3 µF metallized film capacitor and 10 ohm resistor are good starting values for the snubber. Figure 2(e) shows the effects of adding a snubber and Figure 2(f) shows a snubber plus free wheeling diode.

Summary

EMI can be minimized in low speed relay or solenoid control designs by adding a RC filter to the gate drive to slow down the power transistor's switching times and a RC snubber across the load to contain the inductive "kickback" voltage. \doteq



Graph 1. Switching delay from adding gate capacitor



Figure 2(f). Adding a 0.33 μF 10 Ω snubber to the free wheeling diode along with 0.1 μF gate capacitor minimizes EMI.



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Rugged EMF Meters Deliver Precision and Portability

This article describes the new line of EMF meters from Wandel & Goltermann, as featured on the cover of this issues. For more information, contact Wandel & Goltermann at 2200 Gateway Centre Blvd., Morrisville, NC 27560-9228; Tel: (804) 491-5047. Fax: (804) 491-3163: or circle Info/Card 182.

Safety in electromagnetic fields (EMF) is an issue which has carved out a place of its own in the news, with a particular focus on workplace safety. In response to growing concern, Wandel & Goltermann has introduced a family of EMF meters that can be used to make quick, precise measurement of fields in nearly any workplace.

Dealing With "Electrosmog"

Although an artificial term, the term *electrosmog* is becoming commonly used to describe the environmental impact of being constantly exposed to electromagnetic fields. Although blown out of proportion in the press, research of the late 1970s brought legitimate concerns to light regarding the effects of omnipresent fields on man and the environment.

It has been determined that electromagnetic fields

have an effect on the human organism. Thermal effects are relatively straightforward, relating to the heating of the water in our bodies. One danger of this type of temperature rise is that the human temperature control mechanisms are normally triggered by sensors in the skin. EMFinduced heating occurs internally, where the water content is highest. As a result, sweating and other protective reactions do not occur.

Non-thermal effects have also been noted, in particular, experiments show changes in the permeability of cell membranes and changes in the phagocytic activity of lymph nodes. It is likely that high frequency radiation of a given intensity and modulation weakens the immune system, affects the hormone balance, and may even have psychological effects.

Although debate continues on exactly what field intensities cause what degree of harm, standards have been developed that address the dangers as we understand them. Studies are ongoing, and these standards will undoubtedly change in future as more research is completed.



Wandel & Goltermann's new line of EMF meters: Model EFA-1 and EFA-2 have the case style on the left; the EMR-10 and EMR-11 style is shown in the center; the EMR-20 and EMR-30 are as pictured on the right.

Sources of EMF

Low frequency EMF appears mainly as magnetic fields where large currents flow and conductors are separated or magnetic operation is involved. Devices include electric arc welding equipment, motors and power supplies. Low frequency electric fields occur in open multi-plug installations and extension cables. Measurements can determine whether hazardous fields are present at a given location.

High frequency EMF (radio waves) occurs in many places. The highest levels will be found near radio and television stations and satellite earth stations. Safety zones and limited exposure times are part of a protection plan. Also of concern are the many low power radio devices, such as cellular telephones, which can have high field intensities very close to the units. Precision measuring instruments are needed to identify areas to avoid, and to verify that protected areas are indeed safe.

In addition to communications equipment, radio energy is commonly used in industry for lo-

New EMF Meters

calized heating and plasma generation (sputtering or vaporizing). Some medical equipment makes use of high intensity radio energy, as well. Employee safety is especially important, since workers are near the ecuipment for long periods of time. Mcnitoring the fields created by electronic equipment with accurate, reliable instruments is an essential part of an EMF safety program.

EFA-1 and EFA-2 -**Magnetic Field Analyzers**

Covering magnetic fields from 5 Hz to 30 kHz, the Wandel & Goltermann EFA-1 and EFA-2 analyzers are compact, battery-operated units. They use a built-in three-dimensional magnetic probe, or an optional precision H-field probe that conforms to IEEE and VDE standards. A miniature probe is available that can get into tight spaces. The probes have measurement range of 100 nT to 10 mT, and provide either the RMS or peak values.

The fields can be analyzed by frequency. The units have a wide array of filters, including 5 Hz to 2 kHz, 5 Hz to 30 kHz, and 30 Hz to 30 kHz. The EFA-2 allows individual filter frequencies of 15 Hz to 2 kHz tc be specified by the user. The EFA-2 also has datalogging capability for long-term measurements up to 24 hours, and it will store up to four complete measurement setups, with automatic selection of measurement range. The instruments measure $7.875 \times 4.375 \times 2.375$ inches and weigh 2.2 lb.

EMR-10 and EMR-11 -**High Frequency Monitors**

The EMR-10 measures magnetic fields from 30 kHz to 30 MHz, and the EMR-11 measures electric fields from 100 kHz to 3 GHz. Each one is designed for rugged use in the field by non-technical operators. The measurement ranges and operating parameters of both instruments are optimized to conform to requirements of the International Radiation Protection Association (IRPA), World Health Organization (WHO), and national organizations such as IEEE/ANSI, IEC and NRPB. Both instruments will collect measurement data and transfer that data to a computer via the built-in RS-232C interface. The units have an alarm with user-adjustable threshold, instantaneous or average measurement, and automatic self-diagnostics. Measurements are displayed in V/m, A/m, mW/cm², or W/m². Instrument size is $3.5 \times 1.75 \times 9.5$ inches, and the weight is 12 oz.

EMR-20 and EMR-30 -**Precision Hand-Held Instruments**

Models EMR-20 and EMR-30 are hand-held E-field radiation meters for 100 kHz to 3 GHz measurements. They are suited for applications such as servicing of RF communications equipment and use in RF radiation safety programs at industrial and manufacturing facilities. Measurement accuracy is exceptional, based on proprietary triaxial signal processing circuitry. The units come with an isotropic omni-directional probe providing 60 dB dynamic range. The units contain a built-in optical interface that allows easy calibration by the owner, or through the facilities of recognized calibration laboratories. The EMR-30 will internally story sets of measurements including value, time stamp and instrument setting. Both units measure $3.75 \times 2 \times 18$ inches (including probe), and weigh 1 lb.



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Cobalt-based amorphous alloy MAGNAPERM® high permeability cores from AlliedSignal Amorphous Metals are designed with an extremely flat DC hysteresis loop. Permeability greater than 90,000 at 1 kHz makes these cores particularly effective for noise suppression applications. In addition to EMI common mode filtering, applications also include telecommunications and data communications interface transformers. pulse and current transformers. AlliedSignal

Amorphous Metals Parsippany, NJ Info/Card #168

Filtered D-Sub Connectors

Power Dynamics line of D-Sub connectors are designed to suppress EMI/RFI noise over a wide range of frequencies. The units include integrated ferrite plates to combine a filter/connector into a single space-saving unit. The connectors are available in 5.0 mm, 7.2 mm, 9.4 mm and 13.84 mm footprints, and meet EIA, RS-232C and RS449 standards. Terminations available include p.c.b., solder cup, crimp and I.D.C.

Power Dynamics, Inc. West Orange, NJ Info/Card #170

Suppressor Diodes

Semtech Corporation announces a new familty of transient voltage suppressor (TVS) diodes designed to protect sensitive ICs from damage due to ESD. The new devices are provided in low-cost SOT-23 packages. The diodes use a dualjunction, common anode configuration and can be used to protect two uni-directional lines or one bi-directional line, making them application to signal lines as well as the V_{cc} bus. Models are available in standoff voltages of 5, 12, 15 and 24 V. In 10,000 quantities, the price is 0.39 each. Semtech Corporation

Newbury Park, CA Info/Card #171

Custom Filters

Elpac Components announces a line of custom EMI filters. Filters can be tailored to specific filtering needs in high-reliability applications such as industrial controls, aerospace and mobile electronicc where high power and signal level curretns must operate independently without crosstalk. Elpac Components Irvine, CA

Info/Card #169

Shielding

PTFE Coated Shielding Foils

Custom fabricated PTFE coated foils have been introduced by Insul-Tab, Inc. for use as release liners in manufacturing, EMI/RFI shileds in electronics, and in food packaging applications. Aluminum, copper and stainless steel foils can be supplied, with foil thicknesses of 1 to 15 mils, and widths from 1/2 inch to 18 inches. Insul-Tab, Inc. Woburn, MA

Info/Card #172

Vacuum Metallization Capabilities

Rare Earth Coatings offers vacuum metallization for EMI/RFI shielding and reflective applications. Their Vacuglas[®] process deposits metal onto plastic materials with strong adhesion, providing a minimum 1 ohm per square and 72 dB continuous. Several different metals can be applied: copper, aluminum, silver, gold and others.

Rare Earth Coatings West St. Paul, MN Info/Card #173

Connector Gaskets

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Microwave Amplifiers

A new line of broadband microwave amplifiers have been introduced by Amplifier Research, intended for susceptibility and general laboratory applications in the L, S, C, X and IJ bands. Three solidstate models provide 1, 5 and 10 watts minimum output from 1.0 to 4.2 GHz, and four TWT amplifiers provide 200 watt output from 1-2 GHz, 2-4 GHz, 4-8 GHz, and 8-18 GHz, respectively. The amplifiers feature reduced power output under mismatch condition rather than shutoff, for uninterrupted testing. All amplifiers are rated at minimum power output at the output connector, rather than "typical" or "nominal" specifications. A complete set of protection features, gain control and and IEEE interface are provided.

Amplifier Research Souderton, PA Info/Card #176

cision die-cut gaskets using Shieldseal 106 sheet materials from James Walker & Co. The nickel-filled silicone elastomer gaskets meet military specifications, and can be provided for a wide range of commonly-used D-type and circular connectors, as well as custom configurations. The gaskets offer 120 dB shielding attenuation and EMP survivability.

James Walker & Co. Woking, Surrey U.K. Info/Card #174

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Tecknit offers their new Teckcell-A (LP) panels, 0.25 inch thick aluminum honeycomb material, providing air flow and EMI shielding performance at a low cost for commercial applications. The vents are available with gasketing of beryllium copper fingers, oriented wires in silicone, or UL-rated nickelplated fabric and neoprene rubber. Optional finishes include chromate conversion, tin & electroless nickel plating.

Tecknit Cranford, NJ Info/Card #175

Equipment

EMI Receiver

Messelektronik Berlin introduces a low-cost portable EMI receiver, featuring built-in PC with memory card and LCD graphic display. The unit operates for four hours on rechargeable batteries. The receiver uses a synthesized local oscillator. preselection, automated attenuators and CISPR Quasi Peak demodulation. IF bandwidths are 0.2, 9.0 and 120 kHz. IEEE interface and opto-coupled RS-232 interface provide convenient test configuration. **MEB Messelektronik Berlin** Berlin, Germany

Info/Card #177

Immunity Tester

the RF power generator system EMCG 230/B2 from Dressler is a complete unit for testing products to the IEC-1000-4-6 standard for conducted immunity. The EMCG 230 has all necessary modules to form a complete test system without requiring separate RF power amplifier, signal generator and

New Products

modulator. As required by the standard. the unit provides 8 watts and drives an integrated 6 dB attenuator to provide a stable 2 watts output. Test frequencies from 0.15 to 230 MHz can be set in 10 kHz increments by front panel thumbwheel switches. CW and the required 1 kHz, 80% AM modulation are provided.

Dressler Hochfrequenztechnik Stolberg, Germany Info/Card #178

Software

3-D EMI Simulation

QUIETTM Version 2.0 is introduced by Quad Design, providing prediction of electric and magnetic field intensities radiated from backplanes, motherboards and MCMs. the new model of this EMI analysis tool includes a 3-D simulation engine that permits the automatic simulation of complex system effects, including cable common mode current and radiation. Multiple board EMI shielding and scattering are also simulated, as is enclosure resonance. Understanding the behavior of these system characterstics is essential to meeting EMC

specifications. **Quad Design** Camarillo, CA Info/Card #179

Literature

EMI Gasket Catalog

Spira offers a new catalog on spiral EMI gaskets and shielding products. Sections include: expanded product data sheets, shielding quality information, groove and surface-mounting guidelines, fastener spacing guidelines, corrosion control information, and custom gasket information. Spira's gaskets come in a wide range of diameters as small as 1/32 inch, provided in either tin/lead plated berylliuym copper or low-cost stainless steel.

Spria Mfg. Corp.

North Hollywood, CA Info/Card #180

ESD Control Products

Charleswater has released their 1995 catalog of static control products and ESD training aids. Products include bags, cleaners, conductive paints, foam, foot grounders, ionization products, mats, laminates, floor finishes, ESD test intruments, workstation materials, wrist straps and many other ESD control items. Books, videos, ESD standards publications and field service kits are also offered in this new catalog.

Charleswater Canton, MA Info/Card #181



EMC Testing Software

System 55TM from IFI, Inc. provides automated EMC testing, offering the capability of determining whether a test room is calibrated for the IEC-801-3 specification. Calibration time can be reduced from days down to hours. The software also automates IEC-801-6, MIL-STD-461/462 and RTCA/DO-160 testing, and others. System 55 will analyze the data it obtains for the IEC-801-3 16-point E-field uniformity matrix and indicates the pass-fail points. It can gather data on antenna, amplifier, sensor and test room performance, while offering extensive control of the testing environment for test flexibility.

IFI. Inc. Ronkonkoma, NY Info/Card #154

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A Review of the Methods for Obtaining the CE Mark

By Gary A. Breed Editorial Director

In order to sell products in Europe, all products will soon be required to have the CE mark, indicating compliance with the requirements of all applicable European Directives. For EMC-related compliance, the EMC Directive and its amendments contain most requirements that must be met. Other Directives that contain EMC requirements include Telecommunications Terminal Equipment, Medical Devices, Motor Vehicles, and a few others. The EMC Directive becomes effective January 1, 1996.

In general, the EMC Directive has a practical purpose. It is intended to assure that products do not cause interference (radiated emissions), and that they can operate without disruption to to interference from other sources (immunity). The immunity requirements contained in the European EMC Directive are the first immunity requirements in the world that apply to all electronic products.

Three methods are available for gaining authority to use the CE mark: Self Certification, Technical Construction File and Type Examination. Each method has differing formal requirements and application to individual devices or families of products.

Self-Certification

As the name indicates, self-certification is performed by the manufacturer of the equipment. A Competent Body (an approved testing laboratory) is not necessarily required, but testing according to the applicable standards *is* required, even if it is done in the company's own laboratory. When testing is completed and the product is determined to be in compliance, a Declaration of Conformance is prepared and included with the product, either on the warranty card or in the manual. Product testing records must be maintained for ten years.

The advantage of Self-Certification is simplicity: a manufacturer that is confident that the product meets all requirements, and has performed sufficient testing to confirm compliance, can simply write the Declaration of Conformance, apply the CE mark and sell the product.

There are two principle disadvantages. The first is that each product and product variant must have its own test sequence and record. If a company makes a large number of similar products, the extra time and cost of separate tests may be excessive (see the next method). The other disadvantage is that, in the case of a complaint or challenge to a product's compliance, the company alone carries the burden of proof. This, of course, is also the factor that prevents companies from falsely claiming Self-Certification and using the CE mark without proper testing; the cost of cheating will be high!

Technical Construction File

This type of certification establishes that the products have been designed and constructed in a manner that assures compliance with EMC standards. Technical product details, usually including testing, are gathered in a design procedure file. This file is reviewed by a Competent Body which may or may not perform additional testing. When the Competent Body approves, the Declaration of Conformance can be prepared and the product sold with the CE mark.

The advantage of a Technical Construction File is that a family of similar products can be covered in one file, which can mean significant overall savings in cost and testing time to some companies. Also, the approval of a Competent Body brings a higher



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Obtaining the CE Mark

level of confidence to consumers and enforcers of EMC requirements. It is likely that this method will be considered "stronger" than self-certification, and will be used by some companies to present an image of higher quality.

The disadvantage is cost and complexity. Documentation includes considerably more information than compliance testing results. In addition, the use participation of an outside party (the Competent Body) can significantly increase the time and cost required to complete the approval process.

Type Examination

This method certification is primarily reserved for very high importance products with the potential for widespread EMC effects. Radio and television transmitters are probably the main subjects for Type Examination. This method parallels current methods for approving these types of equipment. For many years, numerous countries have had separate performance requirements for communications transmitters. In some cases, these separate requirements are being maintained, but they are modified to use the EMC Directive as the defining standard for the EMC portion of those performance standards. Type examination is performed by a Notified Body, which may be a national regulatory agency or a testing laboratory specifically designated to act on the agency's behalf.

Summary

Obtaining the authorization to affix the CE mark and sell a product in Europe has three routes (two for most products). The early debate over potential protectionism through difficult certification procedures has ended with the clarification of the above procedures. Of most concern is the potential difficulty in achieving compliance with the EMC standards. The emissions standards are similar to those of the VDE and other individual countries, but the immunity standards include radiated and conducted RF, ESD, EFT and surge requirements that are completely new to most companies. It is the goal of the European Community to have more robust electrical and electronic products enter their markets, to avoid most problems due to interference and common powerline disturbances.

Future Trends

Countries around the world will be observing the operation of the European Union compliance process. Most developed countries have made some commitment to harmonization of regulations; not only for EMC, but for safety and other areas, as well. Especially important is immunity testing and compliance. In this area, Europe has taken the lead, forcing electronics manufacturers to make their products resistant to the detrimental effects of external fields and currents.

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RF filter design

Microstrip Coupled-Line Bandpass Filter Synthesis and Analysis Program

By Sean R. Mercer, Ph.D., Racal Canada, Eric Mabada, University of Cape Town

Program BPF.BAS greatly simplifies the task of microstrip coupled-line bandpass filter design. Simply enter the desired performance characteristics of your filter and the program will synthesize the dimensions of the filter to meet the specified criteria. A simple analysis procedure provides tabular and graphical output and you can generate a file for HP-EEsof's Touchstone or Compacts Software's Super-Compact for further analysis. Filters synthesized using this program are, however, accurate enough to be used in many applications without any modification.

The process of filter synthesis using LC ladder or impedance inverter prototypes is well understood and there are many excellent texts describing the design or development of these filters [1,2,3,4]. The development of microstrip synthesis procedures for resonators such as coupled lines [5] has made it possible to create microstrip filters based on the prototype filters. The use of Chebychev prototype filters to create microstrip coupled line filters has been well documented [6]. However, this design procedure is a lengthy one, and an automated technique is preferable. Program BPF.BAS is coded in QBASIC and provides an automated solution to the design of microstrip coupled-line bandpass filters.

Both series and parallel resonators would be required to directly realize a bandpass filter from an LC ladder prototype filter. A microstrip resonator topology (coupled lines) can be arranged to exhibit either series or parallel resonance. Different resonator topologies are required for series and parallel resonators. However, if an impedance-inverter coupled lowpass prototype filter is used for bandpass filter synthesis, only one type of resonator is required. This greatly simplifies the filter topology by eliminating the need for shorted conductors and the associated complications with modeling and fabrication.

One of the factors limiting the achievable bandwidth with a coupled line filter is the amount of coupling possible between the lines forming the resonators. End-coupled or parallel-coupled lines are realizable in microstrip. The parallel-coupled line topology offers greater coupling than the end coupled line topology. Wider bandwidth designs are therefore possible with the parallel-coupled line topology.

The bandwidth performance of this coupled line bandpass filter topology is limited by realizable resonators. When the required bandwidth exceeds 15 percent it is often not possible to realize microstrip coupled-line resonators with the required odd and even mode impedance values. For this reason, this microstrip filter topology is usually limited to designs requiring less than 15 percent bandwidth. However,



Figure 1. Bandpass filter with three coupled line sections.

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Figure 2. Sample input data for the program.

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•*LP-2.5	DC-2.5	3.8-5.0	5.0-200	★LP-250	DC-22
*LP-5	DC-5	8-10	10-200	*LP-300	DC-27
*LP-10.7	DC-11	19-24	24-200	★LP-450	DC-40
*LP-21.4	DC-22	32-41	41-200	★LP-550	DC-52
*LP-30	DC-32	47-61	61-200	★LP-600	DC-68
*LP-50	DC-48	70-90	90-200	★LP-750	DC-70
*LP-70	DC-60	90-117	117-300	★LP-800	DC-72
*LP-90	DC-81	121-157	157-400	★LP-850	DC-78
*LP-100	DC-98	146-189	189-400	★LP-1000	DC-90
*LP-150	DC-140	210-300	300-600	★LP-1200	DC-10

All models priced qty. 1-9 (Sea.), Conn. Type P = 11.45, B = 32.95, S = 34 ● Exceptions: ★LP-1.9 P = 13.95, B = 34.95, ★LP-2.5 P = 14.95 B = 35.95 On both models, add following to B price: \$3.00 for N, \$2.00 for S

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dc to 108MHz

Model

dc to 1200MHz DC-135 DC-190 DC-225 DC-380 DC-420 DC-550 DC-700 DC-700 DC-1000 DC-5.0 DC-8.0 DC-11 DC-22 DC-25 DC-30 DC-30 DC-45 DC-95 8-10 12.5-16.5 19-24 32-41 36-47 SCLF-135 SCLF-190 SCLF-225 SCLF-380 SCLF-420 10-200 16.5-200 24-200 41-200 47-200 SCLF-5 SCLF-8 SCLF-10.7 210-300 290-390 340-440 390-800 390-800 440-1200 750-1800 920-2000 1050-2000 1300-2000 2100-2500 SCLF-21.4 SCLF-25 SCLF-30 580-750 750-920 47-61 61-200 SCI E-550 800-1050 SCLF-700 SCLF-1000 1000-1300 SCLE-45 70-00 90-200 146-189 189-400 SCLF-95 Price: SCLF 21.4-SCLF 420 \$11.45 ea. SCLF-8, 10.7, 550, 700, 1000 \$12.95 ea. SCLF-5 \$14.95 Qty. (1-9)

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	Passband MHz	Stor	oband IHz	Freq. Ra	/SWR nge, DC thru	Group Freq	Delay Variat Range, DC	ions, ns thru
No.	loss < 1.2dB	loss >10dB	loss >20dB	0.2fco X	0.6fco X	fco X	2fco X	2.67fco X
★BLP-39 ★BLP-117 ★BLP-156 ★BLP-200 ★BLP-300 ★BLP-467 ▲BLP-933 ▲BLP-1870	DC-23 DC-65 DC-94 DC-120 DC-180 DC-280 DC-560 DC-850	78-117 234-312 312-416 400-534 600-801 934-1246 1866-2490 3740-5000	117 312 416 534 801 1246 2490 5000	1.3:1 1.3:1 1.3:1 1.6:1 1.25:1 1.25:1 1.3:1 1.45:1	2.3:1 2.4:1 1.1:1 1.9:1 2.2:1 2.2:1 2.2:1 2.9:1	0.70 0.35 0.30 0.40 0.20 0.15 0.09 0.05	4.0 1.4 1.1 1.3 0.6 0.4 0.2 0.1	5.00 1.90 1.50 0.80 0.55 0.28 0.15

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high pass, Plug-in, 13 to 1200MHz

210 to 2200MHz I Desehond I VOWD ~ . . . I Deserved LVOWD

	M	-Iz	MHz	Pass-	1.000	M	Hz	MHz	Pass-
Model No.	loss > 40dB	loss > 20dB	loss < 1dB	band Typ.	Model No.	loss >40dB	loss > 20dB	loss < 1dB	band Typ.
*HP-25 *HP-50 *HP-100 *HP-150 *HP-175 *HP-200 *HP-250 *HP-300	DC-13 DC-20 DC-40 DC-70 DC-70 DC-70 DC-90 DC-100 DC-145	13-19 20-26 40-55 70-95 70-105 90-116 100-150 145-190	27.5-200 41-200 90-400 133-600 160-800 185-800 225-1200 †290-1200	1.7:1 1.5:1 1.5:1 1.8:1 1.5:1 1.6:1 1.3:1 1.7:1	*H ² -400 *H ² -500 *H ² -600 *H ² -700 *H ² -800 *H ² -900 *H ² -900 *H ² -900	DC-210 DC-280 DC-350 DC-400 DC-445 DC-520 DC-550	210-290 280-365 350-440 400-520 445-570 520-660 550-720	395702 5001800 700-1800 780-2000 910-2100 1000-2200	1.7:1 1.9:1 2.0:1 1.6:1 2.1:1 1.8:1 1.9:1

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Model No.	Center Freq. (MHz)	Passband I.L. 1.5 dB Max. (MHz)	3 dB Bandwidth Typ. (MHz)	I.L. > 20dB at MHz	pbands I.L. > 35dB at MHz
*BP-10.7 *BP-21.4 *BP-30 *BP-60 *BP-70	10.7 21.4 30.0 60.0 70.0	9.5-11.5 19.2-23.6 27.0-33.0 55.0-67.0 63.0-77.0	8.9-12.7 17.9-25.3 25-35 49.8-70.5 58.0-82.0	7.5 & 15 15.5 & 29 22 & 40 44 & 79 51 & 94	0.6 & 50-1000 3.0 & 80-1000 3.2 & 99-1000 4.6 & 190-1000 6.0 & 193-1000
Price, (1-9	ety), all	models: plug-	in \$18.95,		

BNC \$40.95, SMA \$42.95, Type N \$43.95

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Model No.	Freq. MHz	MHz loss < 1dB	loss > 20dB at MHz	1:3:1 Total Band MHz
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★IF-30	30.0	25-35	1.9 & 210	DC-330
★IF-40	42.0	35-49	2.6 & 300	DC-400
★IF-50	50.0	41-53	3.1 & 350	DC-440
★IF-60	60.0	50-70	3.8 & 400	DC-500
★IF-70	70.0	58-82	4.4 & 490	DC-550

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DIELECTRIC THICKNESS =

CONDUCTOR THICKNESS = PERMITTIVITY ER

0.635 mm 0.0004 mm 9.90

REQUIRED FILTER DEGREE = 8

WIDTH of a 50 Ohm feed line is 0.614 mm.

PRESS ANY KEY TO VIEW FILTER DIMENSIONS

Figure 3a. Synthesized filter parameters - page 1.

CALCULA	TED COUPLEI	D LINE DIMENSIONS in mm
WIDTH	SPACING	LINE LENGTH
========		======
0.567	0.090	3.542
0.771	0.553	3.436
0.779	0.77	3.421
0.781	0.830	3.419
0.781	0.842	3.418
0.781	0.830	3.419
0.779	0.777	3.421
0.771	0.553	3.436
0.567	0.090	3.542

PRESS ANY KEY TO VIEW FILTER DIMENSIONS

Figure 3b. Synthesized filter parameters - page 2.

there are techniques available to improve the bandwidth performance of this type of filter [8,9].

A diagram of a parallel coupled line microstrip bandpass filter with three coupled sections is shown in Figure 1. The conductor widths and spacings are clearly shown.

The effects of dispersion in microstrip and the frequency dependence of the microstrip effective permittivity ε_{eff} , are also calculated in this program [7] to improve the accuracy of the calculated filter conductor dimensions.

An overview of the method used in program BPF.BAS to synthesize microstrip parallel coupled line bandpass filters is given below:

1. Specify the filter design parameters.

2. Determine the required filter order.

3. Calculate the impedance inverter prototype filter values.

4. Calculate the required odd and even mode impedances for the coupled line resonator sections.

5. Synthesize the coupled line resonator sections by determining the strip width to substrate thickness (w/h) and strip separation to substrate thickness (s/h) ratios for each resonator. An iterative technique is used to determine the final line widths and spacings for the coupled line sections.

6. Output the computed filter dimensions.

Program Operation

The user is prompted to enter the desired filter characteristics, namely passband return loss, stopband rejection and selectivity. Filter selectivity is defined as the bandwidth at which the desired stopband attenuation is achieved divided by the filter 3 dB bandwidth. The desired filter center frequency and 3 dB bandwidth are also entered. The substrate dielectric thickness, dielectric constant and conductor thickness are the final inputs required before filter synthesis will begin.

Typical input data for the program is shown in Figure 2. The data shown in Figure 2 represents a filter with 10 percent bandwidth with a center frequency at 8 GHz. The substrate parameters are for 0.635 mm (25 mil) alumina with $\epsilon_{r} = 9.9.$

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Figure 4a. Filter return loss.

The required number of resonators is then calculated and the impedance inverter prototype filter values are determined. The odd and even mode characteristic impedances for the parallel-coupled microstrip resonators are then computed. The line width to substrate height (w/h) and strip separation to substrate height (s/h) ratios are calculated for each resonator. An iterative technique is used to determine the final value for the s/h ratio for each resonator.

Program output consists of the number of resonators and the strip parameters of width, length and separation. The width of a 50 ohm line, used as input and output feed lines, is also computed for convenience.

A simple analysis of the filter performance over a user selected frequency range and step width is computed by multiplying the transfer matrices of the coupled line resonators together. The final "ABCD" transfer matrix for the filter is used to compute the insertion loss, return loss and group delay of the filter at each frequency point. The use of "ABCD" transfer matrix parameters is explained in detail in [1,4] and [10]. The analysis method used here is similar to a previously published routine [11].

The user can opt to analyze the filter performance over a number of different frequency ranges before viewing graphs of data over the last frequency range selected. The synthesized filter dimensions and all tabular listings of analysis data for all selected frequency points are written to a text file. This text file has a default name of "RESULTS.TXT" that can be changed by the user if desired.

The synthesized filter data are outputted on two screen pages and to the "RESULTS.TXT" file. The results calculated by the program for the input data given in Figure 2 are shown in Figure 3a and Figure 3b.

Comparison of Results with

Proprietary Analysis Packages Tabular and graphical output of return loss, insertion loss and group delay is provided over the user defined frequency range. This analysis is approximate and we suggest using a comprehensive analysis package such as Touchstone or Super-Compact to verify the filter performance if a center frequency accuracy of better than 1.5 percent is required. To this end, the program will generate either a Touchstone or a Super-Compact ".CKT" file for the user. These analysis packages consider the open-end effects of the open circuit resonators and the effects of step discontinuities in the filter structure.

Graphical outputs from program BPF.BAS, Touchstone and Super-Compact are compared in Figure 4a and Figure 4b. These results are for the filter data shown in Figure 2, Figure 3a and Figure 3b. The data indicates that the actual filter center frequency is slightly lower than that predicted by the simple analysis procedure in program BPF.BAS. This is largely due to the superior modeling of the open-ended line effect and step discontinuities included in the Touchstone and Super-Compact filter analysis.



Figure 5a. Return loss for 2.4 GHz filter

Further results for filters of different bandwidths are shown in Figures 5a and 5b and Figures 6a and 6b. A 0.635 mm (25 mil) softboard substrate with $\varepsilon_r = 10.5$ was used for the design shown in Figure 5 and a 0.635 mm (25 mil) alumina substrate with $\varepsilon_r = 9.9$ was used for the design shown in Figure 6. It is clear that program BPF.BAS produces results that are within 2 percent accuracy of the proprietary analysis packages.

It is a simple matter to optimize the lengths of the open circuit resonators to shift the resonant frequency upwards by 1 - 2 percent. A filter with passband center frequency of 9 GHz was constructed using 0.635 mm (25 mil) Alumina with $\varepsilon_r = 9.9$. The filter was modeled using the same Touchstone model that is generated by program BPF.BAS. The actual filter center frequency was within 1.2 percent of that predicted by Touchstone.

It can be seen from the above information that, for many applications, program BPF.BAS is more than accurate enough to produce filters without the need for checking with one of the proprietary analysis packages.

Computer Requirements and Program Run Time

The program BPF.BAS will run



Figure 5b. Insertion loss for 2.4 GHz filter



Figure 6a. Return loss for 8 GHz filter with 15% bandwidth



Figure 6b. Insertion loss for an 8 GHz filter with 15% bandwidth.

under DOS version 5 or later (QBASIC interpreter). VGA (or better) graphics are required. The computation time to synthesize the coupled line sections varies depending on the required filter order and bandwidth. On a 486DX2-66 PC the approximate computation time for the filter specified in Figure 1 (eight coupled line sections) is eighteen seconds.

Some Practical Hints

The first and last coupled line sections of a bandpass filter of this type are usually tightly coupled. This means that the coupling gaps between these conductors are relatively small. If you are working or softboard or PCB material, ensure that the chosen conductor thickness and fabrication process are suitable for achieving repeatable results with the required conductor and gap dimensions. Remember that thick conductors are prone to undercut in the etching process and filter response is sensitive to changes in the gaps between the printed lines.

The bandwidth of a parallel coupled line section filter is very sensitive to the separations of the first and last coupled line sections. The filter bandwidth can be reduced by slightly increasing the separation of these line sections.

The filter center frequency is strongly influenced by the length of the cou-

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A word of caution to the inexperienced designer. All of the analysis methods mentioned above predict very high values of stopband attenuation at frequencies far from the passband. In practice, however, it is very difficult to achieve isolation greater than 70 dB [12]. This high practical value of isolation usually requires excellent mechanical isolation and very careful attention to circuit layout.

Concluding Remarks

Program BPF.BAS provides quick and accurate synthesis of microstrip coupled line bandpass filters. The designs are accurate enough to use without modification in many applications but results can easily be compared to those from expensive proprietary packages.

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Info/Card #163

Semiconductors for Wireless

M/A-COM announces the MD54-0001, the first in a series of passive GaAs mixers with the performance of a diode ring, but in a low-cost SOIC-8 plastic package. Also introduced is the MA4T6325 low voltage, high f_T silicon transistor for 3 V battery operation, featuring 1.5 dB NF at 1 GHz. M/A-COM

Booth 401 Info/Card #164

Phase-Locked Multipliers

Techtrol Cyclonetics introduces the PLX800 series and PLX1400 phase locked multiplier products. The PLX1400 featured a noise floor of -130 dBc at 50 kHz offset at X-band frequencies.

Techtrol Cyclonetics, Inc. Booth 417 Info/Card #165

Integrated Software Package

Eagleware has released GENESYS, an integrated set of programs to assist analog, RF and microwave circuit designers. A high-speed linear circuit simulator is included, along with synthesis tools and a schematic interface.

Eagleware Booth 518 Info/Card #166

Microwave Power Amplifiers

Broadband power amplifiers covering 1-18 GHz using 200-watt TWTs are available in four models from Amplifier Research. Full monitoring, protection and IEEE interface capabilities are included. Amplifier Research Booth 500 Info/Card #167

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Richardson Electronics, Ltd., 40W267 Keslinger Rd., LaFox, IL 60147 SV Microwave, 3301 Electronics Way, West Palm Beach, El. (407) 840-1800	(800) 348-5580 D. Fax (407) 844-8551
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olyphaser Corp., P.O. Box 9000, Minuen, NV 69423	/1/0, (/02) /82-2511
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Dow-Key Microwave Corp., 1667 Walter St., Ventura, CA 93003	(805) 650-0260
Aatrix Systems corp., 5177 N. Douglas Fir Rd., Calabasas, CA 91302	(818) 222-2301

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Glasteel Industrial Laminates, P.O. Box 910, Collierville, TN 38027	TELEMETRY SYSTEMS & ENGINEERING
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Linhtning Arrestors
Fischer Custom Communications 2905 W. Lomita Blvd. Torrence, CA 90505

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Rantec, P.O. Box 1546, Austin, TX 78767	.(512)	835-4684
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Rantec, P.O. Box 1546, Austin, TX 78767	(512)	835-4684
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Antenna Research Associates, Inc., 11317 Fredrick Ave., Beltsville, MD 20705	(310)	937-8888
EMCO, P.O. Box 1546, Austin, TX, 78767	(512)	835-4684
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A.H. Systems Inc., 9710 Cozy Croft Ave, Chatsworth, CA 91311(818) 998-0223 Fax	(818)	998-6892
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Current Probes	· · ·	
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Pulse Surge Transient FSD Hubrid Generators
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TREK INC., 3932 Salt Works Rd., P.O. Box 728, Medina, NY. 14103
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Specialty Technical Components Inc. P.O. Roy 2106 Southeastern Pa 19300 (610) 647-0000
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Conductive Fiber/Fabric
Venture Tape Corp., 30 Commerce Rd., Bockland, MA 02370 (617) 331-5900

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Magnetic Shielding	
Ad-Vance Magnetics, Inc., 625 Monroe St., Rochester, IN 46975	(219) 223-3156
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Tripods	
EMCO, P.O. Box 1546, Austin, TX. 78767	
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TUV Product Service, Inc., 1775 Old Hwy. 8, New Brighton, MN 55112	
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RF software

EM Analysis

The MacNeal-Schwendler Corporation has announced the release of MicroWave-Lab, a 3-D electromagnetic analysis system for high frequency applications such as resonators, as well as microstrip and waveguide components. MicroWaveLab, using edge elements and absorbing boundaries, calculates important network parameters such as scattering matrices, port impedances and propagation constants. The program is available now on both the popular Unix-based workstations and multi-processing supercomputers. MacNeal-Schwendler Corp. INFO/CARD #190

Integrated Circuit Analysis

HP EEsof has released a new version of the HP integrated circuit characterization and analysis program (IC-CAP) modeling suite, which achieves a higher level of automation than ever before. The software provides three new device models and enhanced device modeling capability. IC-CAP version 4.4 supports the following models: EEFET3 GaAs FET model, EEHEMT GaAs HEMT model, and EEBJT2 BJT model. In addition, enhancements have been made to the BSIM 3 model extraction procedures. The new version also includes new instrument drivers. IC-CAP 4.4 is priced at \$31,000, the new models are purchased separately and are priced at \$4,080 each. **HP-EEsof**

INFO/CARD #189

Component Synthesis

MODELMAKER is a component synthesis tool kit for SpiceAge*4W. It includes tools for creating op amp, transformer, attenuator and bipolar transistor simulation models. Using information straight from a supplier's catalog, models are synthesized. While less complex than SPICE models, they are adequate for most applications and calculate many times faster. MODELMAKER is available at \$224 and links with version 3.00 (and later) and Professional Level 3 (and higher) SpiceAge*4W.

Tatum Labs, Inc. INFO/CARD #188

Spreadsheet Analog Simulation

Avista Design Systems introduces Spectre/XL, which embeds circuit simulation inside Microsoft Excel. Spectre/XL's combination of immediate access to all circuit values, and instant "what if" analysis gives analog designers a uniquely flexible tool for evaluating, developing and optimizing circuit designs. The Spectre/XL system supports SPICE3 device models and returns DC (operating point), AC (small signal), or non-linear frequency (spectral) responses. Spectre/XL is priced at \$695 and requires Microsoft Excel 5.0 for Windows.

Avista Design Systems INFO/CARD #187

Schematic Capture

Compact Software has released a new version of Serenade Schematic for the PC. Serenade Schematic 3.0 for Windows includes special high frequency component and layout-oriented symbols that drive Compact's circuit simulation and layout tools. New features include: user-configurable toolbar. integration with Microwave Scope, Harmonica and Super-Compact 6.5, integration with Super-Spice, a new property editor, and userdefined settings.

Compact Software INFO/CARD #186

Spurious Analysis

Orion Software International's Spurious Analysis Professional Version 1.0 for Windows is a spurious frequency and PLL analysis CAE program. The program analyzes single, dual and triple conversion designs for all internally generated spurious frequencies. The PLL section of the program takes the tunable local oscillator values calculated from the analysis done in the spurious frequency section and uses these to determine the value of the N and A counters used in the dual modulus PLL IC. The program is priced at \$229.95 plus \$5.00 S&H.

Orion Software International INFO/CARD #185

NEC2 on Windows

Paragon Technology has released the NEC-WIN Basic antenna modeling package. The software combines the power of the NEC2 core with an intuitive graphical user interface that runs under Windows. With NEC-WIN Basic users can quickly model complex antennas and obtain 2-D or 3-D radiation patterns. NEC-WIN Basic is shipped with a 125-page bound manual, online help and technical support, and has a list price of \$75.

Paragon Technology, Inc. INFO/CARD #184

CAD File Converter

Bay Technology announces CADNEX, a DOS-based CAD file format converter that provides transfer from one CAD file format to another. Import and export GDS-II, DXF, CIF and Gerber files. The converter links mechanical CAD systems to the manufacturing process. In addition to the CAD file converter, a robust graphics editor allows view, edit and plot of imported files. CADNEX is available at an introductory price of \$1,500.

Bay Technology INFO/CARD #183

RF literature

Analog Design Book

Butterworth-Heinemann announces the publication of *The Art and Science of Analog Circuit Design*, edited by Jim Williams of Linear Technology Corp. Jim Williams and sixteen other engineers (plus one physicist) have writter twenty chapters grouped into four major parts: Learning How, Making It Work, Selling It, and Guidance and Commentary. The 392-page hardback sells for around \$49.95.

Butterworth-Heinemann INFO/CARD #206

XMTR Capacitor Catalog

High Energy Corporation's 16-page catalog offers a detailed description of an extensive variety of custom designed and manufactured ceramic RF transmitting capacitors. These capacitors are designed for use in applications requiring high currents, high KVA ratings and working voltages up to 40 kV. Capacitances range from 1 to 10,000 pF. High Energy Corp. INFO/CARD #205

Circulators and Isolators

DITOM Microwave has released a brochure covering their line of circulators and isolators designed exclusively for wireless commercial communications applications. Many of DITOM Microwave's products are low 3rd order intermodulation designs, providing optimum operation over a wide range of power for cellular base station equipment. **DITOM Microwave**

INFO/CARD #193

Chip Capacitor Brochure

Metelics' capacitor brochure provides information on the company's MIS (metalinsulating layer-silicor) chip capacitors. These capacitors, intended for use in hybrid RF and microwave circuits, feature a dual insulating layer, low loss, large pad area for ribbon or multiple bonds, and a very low temperature coefficient. Metelics Corp.

INFO/CARD #200

Catalog Supplement

Elantec introduces its 1995 New Product Supplement, which lists all new analog and mixed signal ICs released or planned for the year. It includes a complete review of new amplifiers, ASIC video devices, power MOSFET drivers and communications ICs. Elantec, Inc. INFO/CARD #192

Switches, Relays and Matrices

K&L/TRANSCO Switch Products announce a catalog enccmpassing all of its newly enhanced capabilties. The 160-page catalog contains three basic sections, K&L standard RF and microwave switches, K&L/TRANSCO standard RF, microwave and waveguide switches, and K&L RF and microwave distribution systems. K&L Microwave, Inc. INFO/CARD #198

Short Form Catalog

RF Products has published a 20-page short form catalog covering its full line of RF and microwave power transistors, 50 ohm unit amplifiers, 50 ohm transistor pallets and high power stripline resistors and terminations.

RF Products, Inc. INFO/CARD #202

Service Information

The latest version of *Bench Briefs* from Hewlett-Packard includes information about a spare parts kit for the HP 8711A network analyzer, timebase ground-loops, and the implications of a clogged fan-filter on metrology instruments. Also included is an instrument service-note index. Hewlett-Packard Co. INFO/CARD #201

Antenna Brochure

Antennaco has released a brochure providing an overview of their complete line of antennas for the wireless communication industry. Included in their antenna line-up are medium-duty and heavy-duty Yagis, omnidirectional and hemispherical antennas, dipoles, PCS/PCN links and antennas for the broadcast industry. Antennaco, Inc.

INFO/CARD #199

RF Book Catalog

Crestone Engineering has published catalog 0795, featuring over 90 books, software products and instructional videos. All catalog selections have been chosen specifically for engineers working in communications systems, circuit design and EMC. Books include classic reference texts as well as the latest releases from 17 different publishers. International service is provided; major credit cards accepted. **Crestone Engineering**

INFO/CARD #197

RF Bandpass Filter Catalog

POLE/ZERO has released a catalog of tunable (solid state) RF bandpass filters. The catalog presents their modular digitally tuned RF filters and preselectors. The 22-page catalog contains information on POLE/ZERO's expanded MINI-POLETM, MAXI-POLETM and POWER-POLETM hopping filters.

POLE/ZERO Corp. INFO/CARD #196

Cellular Products

Microwave Power Devices (MPD) has released a 14-page brochure describing the company's mission and their amplifiers for cellular/PCS applications. Their amplifier lines include Class A, Class AB, Class C and feed-forward amplifiers. Microwave Power Devices, Inc. INFO/CARD #195

RFIC Power Amplifiers

ITT GTC's 40-page RFIC Power Amplifier catalog contains data on seven different power amplifiers for various cellular and ISM band applications, along with package drawings and an application note titled, "Gate Bias Power Control Using MAX853 Negative Voltage Generator." ITT GTC

INFO/CARD #194

Signal Source Catalog

Wavetek announces the release of a new shortform catalog for their Signal Source Technology product line. The catalog provides an overview of Wavetek's benchtop, programmable (GPIB/RS-232) and VXI waveform generation instrumentation. A series of product matrices enable users to easily identify the most suitable models for their applications. Wavetek Corp.

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