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	Freq. Range	(dBc/Hz)	(dBc)	@+12VDC	(Qty.5-49)
Model	(MHz)	SSB @10kHz Typ.	Тур.	Max.	\$ ea.
POS-50	25-50	-110	-19	20	11.95
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/POS-1060	750-1060	-90	-11	30*	14.95
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Max. Current (mA) @ 8V DC. Notes: Tuning voltage 1 to 16V required to cover freq. range, 1 to 20V for POS-1060 to -2000. Models POS-50 to -1025 have 3dB modulation bandwidth, 100kHz typ. Models POS-1060 to -2000 have 3dB modulation bandwidth,1MHz typ. Operating temperature range: - 55°C to +85°C.



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December 1996

featured technology — 3-volt circuits

20 **Bias-circuit methods to reduce** process and temperature variations in GaAs MESFET ICs are compared

In volume production of RF and microwave integrated circuits, a constant quiescent current in response to process and temperature variations is critical for achieving uniform RF performance characteristics. This article examines three methods of biasing GaAs MESFET circuits to reduce the effect of processing and of temperature variations on quiescent current. These include: fixed bias, source resistance feedback and gate- and source-resistance feedback.

Joe Staudinger

cover story

Integrated test solution 30 emulates real-world environment

In wireless communications systems, engineers must take into account various communications channel impairments to adequately compensate with equalization, diversity and error correction. Interference, multipath fading and noise are three impairments that help characterize the wireless channel. These should be used to verify the receiver performance under as realistic a condition as possible. An integrated test solution has been developed that provides the channel impairments called for by cellular, personal communications services (PCS) and satellite communications test specifications.

- Alex Kim

tutorial

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36 The role of digital signal processors in pager technology

Pagers and paging technology have become a major part of the rapidly evolving wireless and mobile communications industry. Advanced paging protocols, including those that support two-way communications, give pager service providers greater capacity to meet the increasing demands for pager coverage and features. These demands present considerable technical challenges to produce products that are competitive both in performance and in cost. Today's state-of-the-art, integrated-circuit (IC) and digital-signal-processor (DSP) technologies, provide effective means to deal with such challenges. As a result, the market will see more sophisticated, cost-effective pagers with more user-friendly features.

-Xiao-an Wang and Dwane Bell

Reducing IM distortion in CDMA cellular telephones

CDMA spread-spectrum technology enables more cellular users to coexist in a given segment of the allocated cellular frequency band. Unfortunately, a problem has appeared in high-density markets where the CDMA systems have been tested. The gremlin is interference caused by intermodulation distortion (IMD) products generated in a CDMA receiver from multiple offchannel analog signals. A fixed attenuator switched in or out at selected RF input levels and positive intrinsic negative (PIN) diodes used as currentcontrolled RF attenuators can reduce IM distortion.

-Dick Bain

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This index lists all articles published by RF Design in the past year. They are organized into major topic categories and listed in chronological order within those categories.



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Coming in January

- Oscillators
- Coil tutorial
- New cover story format: PCS
- The return of the product forum: Transistors

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INFO/CARD 2

RF editorial

What's a designer to do?

By Don Bishop Editorial Director

Designing electronic products to fit regulatory requirements, to meet cost restrictions and to appeal to consumers or industrial users isn't easy. We like to think that RF engineers play a key role in the process—which they do—but consider a manufacturer's perspective.

"We have seen a shift in what makes customers decide to buy our products instead of another manufacturer's," a company president told me. We were talking in the aisle at a trade show. There was plenty of room ... in the aisle ... in his booth ... in everyone's booth. Where were all the engineers? Actually, the sessions were well-attended!

But back to the story.

"Used to be, if you were *nicer* to customers than the next guy, you would win the business," he explained.

What makes the difference now?

"These days, it's 40% price, 40% looks, 15% delivery and 5% technology." Only 5% technology? I'll come back to that.

First, let's consider this matter of *looks*. The company president said that, when he competes for contracts to provide new original equipment manufactuerer (OEM) subsystems, it isn't good enough to provide a version that looks as though it were created in a laboratory. Not even if it works perfectly and looks OK. He said he can lose the business if the prototype doesn't look like a *finished*, manufactured product.

Form over function. Style over substance. Who can deny that appearance is important? Apparently, it isn't enough to leave the matter of appearance to those who design plastic cases and packaging materials. Sometimes the way subassemblies and components look when they reach the customer evaluation stage can make the difference in a sale.

Second, let's think about delivery. To



the company executive, that means everything from actually presenting the finished product to the customer when and where scheduled, to meeting commitments about the product. Commitments might include adherence to specifications, ease of use, ease of installation, durability, suitability and other elements of customer satisfaction.

Third, let's take price into account. Some manufacturers report customer expectations of *declining prices* every year. It isn't sufficient to have the lowest price going in—although that may be critical. Price negotiations may include a sliding *downward* scale with commitments for price reductions over the life of the contract.

Fourth, the characteristic with the lowest-percentage effect on the sale (for this particular manufacturer), *technolo*gy. For all of the pride that may be taken in engineering new products, systems or services (read that: solutions), apparently it accounts for only a small part of the customer decision.

Or does it?

Although the pure technology, the "gee whiz, that works great, glad you thought of that" reaction that we might like our customers to have is one kind of a direct expression of technological success, don't all of the other aspects of the product depend on the engineering, too?

Engineers have to meet the timetables and specifications that allow *delivery*. Selections of components, electronic and mechanical designs, and manufacturing techniques have an enormous effect on *price*. Skill and talent in crafting prototypes (and a willingness to use advice from the right sources) can tip the scale in favor of *looks*.

The 5% that the company president assigns to the technology factor actually calls engineers into play for the other factors as well.

. . .

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RF calendar

- 1997 -

- February 10–14 Wireless Symposium and Exhibition— Santa Clara, CA. Information: Penton Publishing. Tel. 201-393-6256.
 - 23–27 Nepcon West—Anaheim, CA. Information: Reed Exhibition Company, 383 Main Ave., Norwalk, CT 06852-6059. Tel. 800-467-5656; Web site: http://www.nepcon.reedexpo.com.
 - March 3-5 CTIA Wireless—San Francisco. Information: Dobson & Associates. Tel. 202-463-7905.
 - 13–19 CeBIT '97 World Business Center: Office, Information and Telecommunications— Hannover, Germany. Information: Mette Fisker Peterson, Hannover Fairs USA, 103 Carnegie Center, Princeton, NJ 08540. Tel. 609-987-1202; Fax 609-987-0092.
 - 17–20 European Design and Test Conference Paris. Information: Conference Secretariat, CEP Consultants, 43 Manor Place, Edinburgh, EH3 7EB, United Kingdom. Tel. +44-131-300-3300; Fax +44-131-300-3400; E-mail edtc@cep.u-net.com.
 - April 14–17 International Conference on Antennas and Propagation—Edinburgh. Information: ICAP Secretariat, IEE Conference Services, Savoy Place, London WC2R 0BL, United Kingdom. Tel. +44 (0) 71-344-5467/5473; Fax +44 (0) 71-240-8830; E-mail Ihudson@iee.org.uk or mswift@iee.orguk.
 - 21–23 *RF Design* Seminar Series—*Las Vegas.* Information: Intertec Presentations, 6300 S. Syracuse Way, Suite 650, Englewood, CO 80111. Tel. 303-220-0600; Fax 303-770-0253.
 - 22–24 International Wireless Communications Expo--Las Vegas. Information: Intertec Presentations, 6300 S. Syracuse Way, Denver, CO 80111. Tel. 800-288-8606 or 303-220-0600.

RF Pavillion—Manufacturers exhibits within IWCE. Components, test equipment, software and services for RF equipment manufacturing.

- 22–24 Convergence Tech and IC Expo for microelectronics, communications and computer professionals—Dallas. Information: Electronic Conventions Management, 8110 Airport Blvd., Los Angeles, CA 90045. Tel. 800-877-2668, ext. 243; Fax 310-641-5117.
- 23–26 Broadcast Technology—Jakarta, Indonesia. Information: Eileen Lavine, Information Services, 4733 Bethesda Ave., Suite 700, Bethesda MD 20814. Tel. 301-656-2942; Fax 301-656-3179.
- May 5–7 Vehicular Technology Conference for cellular and mobile wireless communications—*Phoenix*. Information: Wendy Rochelle, Registrar, IEEE Conference Service, 455 Hoes Lane, P.O. Box 1331 Piscataway, NJ 08855-1331. E-mail w.rochelle@ieee.org.

- 6–8 Electronics Industries Forum of New England—Boston. Information: Linda Hanson. Tel. 914-779-0696.
- 13–16 Computer and Communication Electronics Design Exposition—Dallas. Information: Reed Exhibition, 383 Main Avenue, Norwalk, CT 06851. Tel. 800-840-5614.
- 28–30 IEEE International Frequency Control Symposium—Orlando, FL. Information: Wendy Ortega Henderson, National Institute of Standards and Technology, Time and Frequency Division, 325 Broadway, Boulder, CO 80303. Tel. 303-497-3593; Fax 303-497-6461; E-mail ortegaw@boulder.nist.gov.
- June 1–5 Supercomm—New Orleans. Information: Telecommunications Industry Association. Tel. 202-326-7300.
 - 9–14 Asia Telecom—Singapore. Information: Tom Dahl-Hansen, senior vice-president, Telecom. Tel. +41-22-730-5298; Fax +41-22-730-6444; E-mail. dahl-hansen@itu.ch.
 - 10–12 International Microwave Symposium and Exhibition—Denver. Information: Horizon House. Tel. 617-769-9750.
 - 11–13 Virginia Tech Symposium on Wireless Personal Communications—Blacksburg, VA. Information: Business Administrator, Jenny Frank, Mobile and Portable Radio Research Group, Virginia Polytechnic Institute, 840 University City Blvd., Pointe West Commons, Suite 1, Blacksburg, VA 24061-0350. Tel. 540-231-2958; Fax 540-231-2968; E-mail hilda@vt.edu; Web site: http://www.ee.vt.edu/mprg/home.html.
- July 14–17 Image Processing and Applications— Dublin. Information: Sheila Griffiths, Conference Organizer, Institution of Electrical Engineers, Savoy Place, London WC2R 0BL, United Kingdom. Tel. +44 (0) 171-344-5475/72; Fax +44 (0) 171-240-8830; E-mail kmoorley@iee.org.uk.
- September 9–11 *RF Design* Seminar Series—Santa Clara, *CA*. Information: Intertec Presentations, 6300 S. Syracuse Way, Suite 650, Englewood, CO 80111. Tel. 303-220-0600; Fax 303-770-0253.

10–12 RF Design '97—Santa Clara, CA. Information: Renie Mayfield, Intertec Presentations, 6300 S. Syracuse Way, Denver, CO 80111. Tel. 800-288-8606 or 303-741-0215.

22–24 Connector and Interconnection Technology Symposium—Anaheim, CA. Information: Chairman, IICIT, P.O. Box 880, Westfield, NJ 07090. Tel. 800-854-4248; Fax 908-233-5116; E-mail IICITDIR@msn.com.

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RFP-150-100RC	GF 3.50	150	DC-2.0	1.20	RFP-150-50TCGF
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RFP-250-100RM	3.10	250	DC-3.0	1.30	RFP-250-50TC
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- Besser Associates-RF and Wireless Made Simple-Jan. 13-14, 1997; Applied RF Techniques I-Jan. 13-17; Modern Computer Communications-Jan. 13-18; RF Impedance Matching and Component Models-Jan. 14; RF Productivity Improvement-Jan. 15-17; RF Smallsignal Amplifiers-Jan. 17; RF Receivers-Jan. 20; EM Field Simulator Made Practical-Jan. 20-21; Antennas for Wireless Applications-Jan. 20-21; EMC and EMI Engineering and Design-Jan. 20-23; Applied RF Techniques II-Jan. 20-24; Wireless RF System Design-Jan. 20-24; RF Oscillators-Jan. 21; RF Mixers and Applications-Jan. 22; Error Correction Coding and Multiple Access Techniques-Jan. 22; RF Power and High-efficiency Amplifiers-Jan. 23-24; RF Measurement Techniques-Jan. 27-30. Information: Besser Associates, 4600 El Camino Real, Suite 210, Los Altos, CA 94022. Tel. 415-949-3300; Fax 415-949-4400; E-mail BesserCourse@delphi.com.
- Celwave University—Marlboro, NJ. Modules offered include: Antenna Basics, Advanced Theory, Towertop Amplifiers, Bidirectional Amplifiers, Filters and Combiners. Information: Gail Magid, Sales Engineering Department, Celwave, 2 Ryan Road, Marlboro, NJ 07746-1899. Tel. 800-235-9283.
- CKC Laboratories—Immunity to ESD—Feb. 3, 1997, Seattle; May 12, Orange County, CA; CE Mark Design and Compliance Routes—Feb. 4–5, Seattle; May 13–14, Orange County, CA; Core EMC Design—Jan. 14–15, Orange County, CA; March 11–12, Fremont, CA; June 17–18, Hillsboro, OR; EMC for Medical Electronics—April 22–23. Information: Linda Grunow or Todd Robinson, CKC Laboratories, 5473-A Clouds Rest, Mariposa, CA 95338. Tel. 800-500-4362 or 209-966-5240; Fax 209-742-6133; E-mail Igrunow@ckc.com.

Georgia Tech Continuing Education—Radar Signal Processing: Theory and Application—Jan. 28–31, 1997; Coherent Radar Performance Estimation—Feb. 3–6; Antenna Engineering—Feb. 3–7; Principles of Pulse Doppler Radar: High, Medium and Low PRF— Feb. 11–13; Introduction to Radar Target Identification—Feb. 25–28. Information: Department of Continuing Education, Georgia Institute of Technology, Atlanta, GA 30332-0385. Tel. 404-894-2547; E-mail conted@gatech.edu; Web site http://www.conted.gatech.edu.

Learning Tree International—Wireless Networks and Mobile Communications—Dec. 17–20, Jan. 14–17, 1997, Feb. 18–21 Washington. Information: Learning Tree International, 1805 Library St., Reston, VA. Tel. 800-850-9197 or 703-709-9119; E-mail uscourses@ learningtree.com; Web site http://learningtree.com.

Mead Microelectronics—Architectural and Circuit Design for Portable Electronics Systems (3-days digital, plus 3-days analog)—March 31–April 5, 1997; RF IC Design for Wireless Communication Systems-May 12–16; Data Communication ICs-May 14–16. Information: Mead Microelectronics, 7100 Grandview Dr., Corvallis, OR 97330. Tel. 541-758-0828; Fax 541-752-1405. In Europe, contact Mead Microelectronics, Venoge 7, 1025 St. Sulpice, Switzerland. Tel. +41-21-691-0244; Fax +41-21-691-0245; E-mail mead@netgate.net; Web site http://www.netgate.net/~mead.

RF Design Seminar Series—April 21–23, Las Vegas; Sept. 9–11, Santa Clara, CA. Information: Intertec Presentations, 6300 S. Syracuse Way, Suite 650, Englewood, CO 80111. Tel. 303-220-0600; Fax 303-770-0253.

Technology International—Achieving and Maintaining Compliance with the Medical Devices Directive— Jan. 14–15, 1997, Denver; Feb. 11–12, Dallas. Information: Kristin Eckhardt, Technology International, 609 Twin Ridge Lane, Richmond, VA 23235, Tel. 804-560-5334; Fax 804-560-5342; E-mail Eckhardt@TechIntl.com.; Web site www.TechIntl.com.

Tektronix—CDMA Modulation Technologies and Measurements; Deploying Digital Transmission in Cabled Networks; TDMA (IS-136 and PCS 1900) Technologies and Measurements—Two-day seminars; Jan. 20–21, Los Angeles; Jan 23–24, Santa Clara, CA; Jan. 27–28, Seattle; Jan. 30–31, Vancouver. Information: Tel. 800-763-3133; Fax 800-835-0025; E-mail TEKFORM2@TEK.COM; Web site http://www.tek.com.

University of Oxford—*RF* and Microwave Design— Jan. 6–10, 1997. Information: Helen Starkey, CPD Centre, University of Oxford, Department for Continuing Education, 67 St. Giles, Oxford, OX1 3LU, United Kingdom. Tel.+44-(0) 1865-288170/3; Fax +44 (0) 1865-288163; E-mail helen.staskey@conted.oxac.uk.

Z Domain Technologies—DSP Without Tears— Jan. 15–17, 1997. Information: Z Domain Technologies, 555 Sun Valley Drive, Suite A4, Roswell, GA 30076. Tel. 800-967-5034 or 770-587-4812. Fax 770-518-8368; E-mail dsp@zdt.com; Web site http://www.zdt.com/~dsp. Other suppliers may promise you quality and reliable service.... Nearson delivers

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IBOC system withdrawn from field testing

AT&T, Lucent Technologies and Amati Communications informed the **Consumer Electronics Manufacturers** Association (CEMA) that they are removing their in-band and on-channel (IBOC) digital audio radio (DAR) system from field-testing consideration because no acceptable testing facility is available. The National Association of Broadcasters (NAB) had agreed to find a San Francisco radio station willing to host the experiments, but was unable to find a volunteer station. The AT&T. Lucent Technologies and Amati Communications IBOC system joins those systems proposed by U.S.A. Digital Radio, which last May also elected to remove its systems from further testing and evaluations.

The events follow the release of laboratory test data last year that revealed poor performance of IBOC DAR systems' audio quality, degradation of the host analog signal, limited digital coverage, and interference caused to existing broadcast stations. Some believe that these results show fundamental design problems with IBOC systems. Proponents say redesigns may be needed, but it is unclear as to whether system changes can cure these critical deficiencies.

Contracts:

Comsat to supply antennas for Sprint PCS project—Comsat RSI Mark Antennas has agreed with Black & Veatch and MFS Network Technologies to supply antennas for the Sprint Spectrum digital wireless personal communications services (PCS) project.

Richardson to distribute Siemens' products—Richardson Electronics has formed a relationship with Siemens Components to distribute Siemens' line of RF and wireless products in North America. Richardson will distribute four key families of Siemens RF products. These include RF integrated circuits, such as phase-locked loops (PLLs), mixers, low-noise amplifiers (LNAs) and modulators; the Siemens grounded emitter transistor (SIEGET) high-speed bipolar RF transistor family; the RF diode family of products such as PIN, varactor and Schottky diodes; and Siemens' gallium arsenide (GaAs) discrete and monolithic microwave integrated circuits (MMIC) components. These products are aimed at such markets as PCS and industrial, scientific and medical bands (ISM)-based technology, as well as cellular and cordless telephony.

Contract for precision compact range reflectors-Electronic Space Systems, Concord, MA, has been awarded a \$1.3 million contract to fabricate and install a precision compact range reflector that will operate at frequencies as low as 300 MHz. Jointly designed by National Aeronautics and Space Administration (NASA) Langley and the Electroscience Laboratory at Ohio State University, the $26' \times 26'$ compact range reflector is intended to demonstrate new technologies in compact range design. It will be used for indoor radar cross-sectional measurements of electrically small reflectors. The new compact range reflector will be smaller in size and will operate at lower frequencies than traditional compact range reflectors.

Business Briefs

FTC facility will increase flip chip capacity—Flip Chip Technologies (FCT), a joint venture between Delco Electronics and Kulicke & Soffa Industries, will open its new production facility in Phoenix, which will quadruple its wafer bumping facility. FCT will use Delco's proprietary Flex On Cap (FOC) solder-bumping process, a technology that has produced more than 300,000 flip chips a day. The new facility will have 36,000 square feet of production and office space and 55 employees.

Anadigics gets clean room—Anadigics is constructing a 10,000-square-foot clean room for the production of gallium arsenide (GaAs) integrated circuits. The clean room will occupy part of the company's new manufacturing space next to its headquarters in Warren, NJ. The expansion will revive a 131,000 square foot building and create more than 250 high-skilled, high-technology jobs. Wafer production capacity will double. The company intends to run 4" GaAs wafers, but the new equipment will be upgradable to 6" wafer production.

Dielectric expands facility—Dielectric Laboratories broke ground for a 23,000-square-foot expansion to its current facility. The addition will allow the company to double its current output of single and multilayer ceramic capacitors, substrates and other passive components for the high-frequency electronics and communications market.

Analog Devices and Sawtek join forces—Analog Devices and Sawtek will collaborate on the development of next-generation infrastructure components for cellular base stations used in global system for mobile communications (GSM) and its variants, PCS1900 and DCS1800. The joint development effort will focus on advanced receiver technology and will result in a new generation of GSM standards-compliant chips and reference designs incorporating surface acoustic wave (SAW) technology.

Xtalonix expands capacity—Previously serving military applications, Xtalonix, Columbus, OH, has expanded its manufacturing capacity to meet the growing private sector demand for high-volume, ceramic-based dielectric resonator materials, ferrites and garnets, typically used in microwave and wireless communication devices.

Ansoft acquires MSC's business unit—Ansoft has acquired the electronics business unit from MacNeal Schwendler for \$5.6 million in cash.

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RF industry insight **RF** in industry

By Ernest Worthman

Earlier this year, Congress, in what may have been one of the most sweeping pieces of legislation of the decade, enacted the Telecommunications Act of 1996. The deregulatory aspects of this act will intimately affect every part of the telecommunications industry. Although it is likely to be several years before the effect of the legislation becomes noticeable, there are already a number of promising opportunities for RF technologies.

For example, it is likely that new technologies such as voice over the Internet, and digital satellite systems (DSSs) will compete for direct access to the home or office, a domain long coveted by the local service providers. Additionally, cable companies will offer both wirelines and wireless telephone services, and telephone companies will offer cable service. It is also likely that the developing technologies such as personal communications services (PCS) and low-earth orbit (LEO) communications will jockey for position in non-traditional markets such as wireless networking.

Depending on who you talk to, there is much speculation that this legislation will be either the second coming or the antichrist. One school of thought is that the big players will gobble up every promising technology, be it RF, data, fiber or whatever and merge into one ubiquitous service provider. On the other side of the fence is the thought that this legislation will force everyone to come to the table and try to work out complementary partnerships where everyone can coexist peacefully.

Either way, the RF industry is likely to benefit for the following reasons.

First of all, this is the '90s, an intense worldwide business atmosphere. Any technology that can support efficiency and cost containment is likely to succeed. Take, for example, radio frequency identification (RFID) and radio frequency data communications (RFDC). One application for RFID and RFDC is to provide real-time, online inventory and process control in manufacturing. This increases inventory accuracy and throughput in warehousing and distribution operations, and it increases productivity on the shop floor. When RFDC systems are integrated with a warehouse management software control system, the results can be linked, worldwide, to other locations or even to other suppliers. And what will the link be? Traditional wireline? Satellite? LEO? PCS? Internet? It is an interesting point to ponder.

Second, the integration of computers and communications (a technology that, a few years ago, I dubbed "computeradio") is a given. Untethered data transmission is the next wave. Just look at the GTE wireless PageCard, for example. In a typical point-to-point transmission, data may flow over any number of wireline or wireless technologies. The future belongs to those who can move information quickly and accurately, whatever the medium. Given the fact that current wireline infrastructure is aging, and bandwidth is limited, it seems logical for business to look to RF for solutions.

And third, unrelated to the telecommunications industy, RF is showing up in unlikely places. RF technology is being used to heat, dry and seal products such as textiles, leather, plastics and ceramics. In these applications it saves money and time over conventional oven-drying methods.

Whichever way it goes, RF's presence in industry is almost assured. Developing digital technologies, a driving thirst for information exchange, the compelling need for a lean, mean manufacturing machine and innovative implementation will see to it.

As a closing note, this will be the last Industry Insight column as you have come to know it. Beginning with the next issue, the industry insight concept will be integrated into the cover story, bringing you timely and pertinent coverage of RF technologies in the brave new world. Having been given the assignment to write many of the 1997 cover stories, I look forward to the challenge of providing RF Design readers with informative, interesting and relevant articles.

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RF circuit analysis

Bias-circuit methods to reduce process and temperature variations in GaAs MESFET ICs are compared

By Joe Staudinger

In volume production of RF and microwave integrated circuits, such as low-noise amplifiers, implementing an integrated-bias method on the circuit to provide a constant quiescent current in response to process and temperature variations is critical for achieving uniform (part-to-part) RF performance characteristics. RF characteristics including gain, noise-figure and efficiency strongly are correlated to the device's quiescent current. Process variances in field effect transistor (FET) threshold voltage, and to a lesser extent in β , usually are the most significant parameters affecting the bias point. The following information examines three methods of biasing gallium arsenide metal semiconductor field effect transistor (GaAs MESFET) circuits to reduce the effect of processing and possibly temperature variations on quiescent current. These include: fixed bias, source-resistance feedback, and gate- and sourceresistance feedback. Both simulation and measured data demonstrate that the latter technique can provide superior performance.

The RF performance characteristics of GaAs MESFET devices are highly sensitive to the quiescent operating condition (primarily the quiescent drain current). For example, noise figure, gain and the device's reflection coefficients vary considerably with quiescent drain current. Thus, in highvolume manufacturing of GaAs MESFET-based circuits, such as lownoise amplifiers (LNAs), achieving uniform part-to-part RF performance requires provisions to account for biasing differences that arise from processing tolerances. Similarly, these characteristics tend to be temperature sensitive as well, and it is desirable to minimize any temperature dependence.

Stabilizing the bias point with GaAs processing and temperature is usually achieved with some type of bias circuit, located either on or off chip. Numerous high-performance, off-chip methods are possible, but cost and size limit their usefulness in commercial applications. Although physically smaller and less expensive, on-chip solutions tend to be based on simpler techniques and thus often exhibit limited performance.

The intent of this work is to benchmark three GaAs MESFET bias-circuit methods suitable for integration on a GaAs monolithic microwave integrated circuit (MMIC) chip. These methods include: fixed bias, source-resistance feedback, and a combination gate and source-resistance feedback technique. All three methods are used in conjunction with a small (400 µm gate width) enhancement mode (positive-threshold voltage) GaAs MESFET. A number of wafers from several lots containing all three circuits were fabricated with significantly varying MESFET parameters, including threshold voltage, gate length and current I_{DSS} . Bias-circuit performance was measured and the results contrasted for each of the three circuit methods.

Process and temperature effects

Some insight into the bias circuit's response to both temperature and process variations can be observed by using a large signal model description of a GaAs MESFET. Based on the selected model, drain current variances can be determined by considering the dependence of the constituent model parameters with processing and temperature. This assumes that model parametric dependence with temperature and process is known, which is a rather extensive characterization task. Even if these dependencies are not known precisely, general bias-circuit performance trends still can be observed.

Certainly a number of large signal MESFET models are available, ranging from physically-based models (those using physical and geometrical properties) to simpler, empirical models, defined by a particular functional form [1]. For simplicity, a traditional empirical model (Curtice) is chosen for this



Figure 1. Effect of β and V₁₀ on the DC I-V characteristics of an enhancement mode GaAs MESFET a) β dependence, and b) V₁₀ dependence.

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	MHz MHz		MHz	Freq. Rang	Freq. Range, DC thru			
Model	loss < 1.2dB	loss	ioss	0.2fco	0.6fco	fco	2ľco	2.67fco
No.		>10dB	>20dB	X	X	X	X	X
★BLP-39 ★BLP-117 ★BLP-156 ★BLP-200 ★BLP-300 ★BLP-467 ▲BLP-933 ▲BLP-1870	DC-23 DC-65 DC-94 DC-120 DC-180 DC-280 DC-560 DC-560 DC-850	78-117 234-312 312-416 400-534 600-801 934-1246 1866-2490 3740-5000	117 312 416 534 801 1248 2490 5000	1.3:1 1.3:1 1.3:1 1.25:1 1.25:1 1.3:1 1.45:1	2.3:1 2.4:1 1.1:1 1.9:1 2.2:1 2.2:1 2.2:1 2.9:1	0.70 0.35 0.30 0.40 0.20 0.15 0.09 0.05	4.0 1.4 1.1 1.3 0.6 0.4 0.2 0.1	5.00 1.90 1.50 1.60 0.80 0.55 0.28 0.15
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NOTE: A -933 and -1870 only with N and SMA connectors.

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Model	Stopt MI- loss	band tz toss	Passband, MHz loss	VSWR Pass- band	Model	Stopi Mi loss	bend Hz loss	Passband, MHz loss	Pass- band
No.	> 40dB	> 20dB	< 1dB	Тур.	No.	>40dB	> 20dB	< 1dB	Тур.
*HP-25 *HP-50 &HP-100 &HP-150 &HP-175 &HP-200 &HP-250 &HP-300	DC-13 DC-20 DC-40 DC-70 DC-70 DC-90 DC-100 DC-145	13-19 20-26 40-55 70-95 70-105 90-116 100-150 145-190	27.5-200 41-200 90-400 133-600 160-800 185-800 225-1200 †290-1200	1.7:1 1.5:1 1.5:1 1.8:1 1.5:1 1.6:1 1.3:1 1.7:1	*HP-400 *HP-500 *HP-600 *HP-700 *HP-800 *HP-900 *HP-1000	DC-210 DC-280 DC-350 DC-400 DC-445 DC-520 DC-550	210-290 280-365 350-440 400-520 445-570 520-860 550-720	395-1600 500-1600 600-1600 700-1800 780-2000 910-2100 1000-2200	1.7:1 1.9:1 2.0:1 1.8:1 2.1:1 1.8:1 1.9:1

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Model No.	Center Freq. (MHz)	Passband I.L. 1.5 dB Max. (MHz)	3 dB Bandwidth Typ. (MHz)	I.L. > 20dB at MHz	pbands I.L. > 35dB at MHz		
*BP-10.7 *BP-21.4 *BP-30 *BP-60 *BP-70	10.7 21.4 30.0 60.0 70.0	9.5-11.5 19.2-23.6 27.0-33.0 55.0-67.0 63.0-77.0	8.9-12.7 17.9-25.3 25-35 49.8-70.5 58.0-82.0	7.5 & 15 15.5 & 29 22 & 40 44 & 79 51 & 94	0.6 & 50-1000 3.0 & 80-1000 3.2 & 99-1000 4.6 & 190-1000 6.0 & 193-1000		
Price, (1-9 city), all models; plug-in \$18,95.							

BNC \$40.95, SMA \$42.95, Type N \$43.95

1.3 & 150 1.9 & 210 2.6 & 300 3.1 & 350 3.8 & 400 4.4 & 490 DC-220 DC-330 DC-400 DC-400 DC-500 DC-500 DC-550 21.4 30.0 42.0 50.0 60.0 70.0 58-82 Price, (1-9 qty), all models: plug-in \$14.95, BNC \$36.95, SMA \$38.95, Type N \$39.95

ssband

MHz

loss

< 1dB

18-25

25-35 35-49 41-58 50-70

Stopband

loss > 20dB

at MHz

VSWR

1:3:1

Total Band

MHz

Constant Impedance.

21.4 to 70MHz

Center Freq.

MHz

Mode

No.

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Figure 2. Clrcuit dlagram of the three bias methods considered. a) voltage-divider, b) source-feedback resistance, c) gate- and source-resistance feedback.

work. Per the Curtice model, drain current is described as a function of intrinsic gate-source and drain-source voltages and four parameters (α , β , λ , and V_{TO}). Thus, we have:

$$I_{ds} = \beta (V_{gs} - V_{TO})^2 (1 + \lambda V_{ds}) \tanh(\alpha V_{ds})$$
(1)

Parameter λ describes the device's output conductance. The α term primarily describes the knee region $(I_{ds} - V_{ds})$. The term V_{TO} defines the threshold voltage. β relates to current gain. If we assume that the device is biased above the knee region (i.e., at V_{ds} of several volts), the two most significant parameters affecting drain current are β and V_{TO} . Figure 1 illustrates the effects that both V_{TO} and β have on the I_{ds} - V_{gs} characteristics of the device. In this case, the device is an enhancement mode MESFET with a nominal threshold voltage of 0.15 V. Changes in either V_{TO} or β can result in significantly different drain currents for a given gate-source voltage.

Bias circuits

We will consider the three circuits shown in Figure 2. The first circuit (Circuit A) is based on a simple voltage-divider method where R_1 and R_2 establish a voltage on the device's



Figure 3. Performance of bias method (Circuit B) due to change in β and V.

gate terminal. The dependence of I_{ds} with β and V_{TO} can be observed by calculating the derivative of Equation 1 with respect to β and V_{TO} . For simplicity, we can assume that the device operates with a drain-source voltage of several volts. If secondary effects from λ and α are neglected, the derivatives are given as:

$$\frac{\partial I_{ds}}{\partial \beta} \equiv \left(V_{gs} - V_{TO} \right)^2$$
⁽²⁾

$$\frac{\partial I_{ds}}{\partial V_{TO}} \cong 2\beta \left(V_{gs} - V_{TO} \right)$$
(3)

The second circuit (Circuit B) is based on using the traditional source feedback resistance Rs connected between the device's source terminal and ground. In addition, because we are considering devices with positive-threshold voltages, a resistive divider network is used to raise the gate voltage above zero. Although the dependence of $I_{\rm ds}$ with β and V_{TO} can be determined in a manner similar to the above, a graphical approach illustrates the performance sensitivity in a simple manner. Figure 3 graphically shows this dependence by plotting the DC load line with the device's I-V characteristics. The intercept of the load with the I_{ds} - V_{gs} curves determines the quiescent current level. Better performance is obtained with this technique compared to the previous method. Additional improvements are possible either by increasing the value of Rs or by raising the gate-voltage offset or both. Be aware that in doing so, the device's drain-source voltage either is reduced or V_{dd} also must be increased (or both) to maintain the same value.

The third circuit (Circuit C) uses a source resistor along with a second FET Q_2 located in the gate-resistor divider network. Device Q_2 is scaled to a small percentage of Q_1 , and resistors R_1 and R_2 are selected such that Q_2 operates at a low drain-source voltage (few tenths). In this manner, Q_2 functions as a variable resistor that is dependent on β and V_{TO} . This can be observed by considering the output conductance of device Q_2 , which by differentiating Equation 1 results in the following:

$$gds = \frac{\partial Ids}{\partial Ids} = \beta (Vgs - VTO)^2 (1 + \lambda Vds) \left(\frac{\alpha}{\cosh^2(\alpha Vds)}\right) +$$
(4)

 $\beta(Vgs - VTO)^2 \lambda tanh(\alpha Vds)$

If both Q_1 and Q_2 are fabricated monolithically (i.e., are on

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ERA-1SM	DC-8000	11.0	13.0	7.0	26	1.85
ERA-2	DC-6000	14.9	14.0	6.0	27	1.95
ERA-2SM	DC-6000	13.1	13.0	6.0	27	2.00
ERA-3	DC-3000	20.2	11.0	4.5	23	2.10
ERA-3SM	DC-3000	19.4	11.0	4.5	23	2.15
ERA-4	DC-4000	13.9	▲19.1	5.2	▲36	4.15
ERA-4SM	DC-4000	13.9	▲19.1	5.2	▲36	4.20
ERA-5	DC-4000	190	▲19.6	4 0	▲36	4.15
ERA-5SM	DC-4000	190	▲19.4	4.0	▲36	4.20

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Figure 4. Performance of bias method C (Circuit CB) due to changes in ß and V.,



Figure 5. Output resistance is plotted as a function of model parameters V_n and β .

the same die and are located in close proximity to one another), then they both are expected to exhibit similar values of β and V_{TO} in response to process tolerances and temperature. The performance of this circuit is illustrated graphically in Figure 4. Again, the DC load line is plotted along with the device's I_{ds} -V_{gs} response. The intercept of the load with the I_{ds} - V_{gs} curves again determines the quiescent current level. On the other hand, although the slope of the DC load line is established by R_s, the gate-offset voltage is deter-

mined by R_1 , R_2 and Q_2 . The output conductance of Q_2 is dependent on parameters β and V_{TO} as described in Equation 4. As is illustrated in Figure 4, if the values of R_1 , R_2 and Q_2 are chosen properly, then:

$$\frac{\partial I_{ds}}{\partial \beta} \cong 0 \quad \text{and} \quad \frac{\partial I_{ds}}{\partial V_{TO}} \cong 0$$

The operation of transistor Q_2 in this bias circuit further can be observed by considering the output conductance g_{ds} given in Equation 4. Figure 5 shows a

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PARAMETER (MEAN)	WAFER A	WAFER B	WAFER C	WAFER D
V _{to}	0.24 V	0.20 V	0.15 V	0.23 V
$I_{ds}@V_{gs} = 0.7$	47.68 mA	45.51 mA	49.95 mA	56.99 mA
GATE LENGTH	0.49 µm	0.55 µm	0.61 µm	0.62µm

Table1. Measured mean parametric values for all three circuits on four different waters.

PARAMETER	CIRCUIT A	CIRCUIT B	CIRCUIT C
IDQ (MEAN, mA)	5.48	5.19	5.21
IDQ (STD mA)	0.90062	0.21181	0.12821
IDQ (MIN)	1.40	4.65	4.94
IDQ(MAX)	4.53	5.63	5.48

Table 2. Circuit comparisons for the wafers used in Table I.



Figure 6. Measured response of each bias circuit to significantly varying FET parametric differences. a) Circuit A, b) Circuit B, c) Circuit C.

plot of output conductance for a given Q_2 device as a function of the relative value of β and V_{TO} . As either β increases or V_{GS} - V_{TO} increases (or both), output conductance g_{ds} decreases, which has the effect of reducing the gate-offset voltage in the bias circuit. It should be noted that in general, V_{TO} and β are not indepdent, but are correlated to some extent.

GaAs MMIC design and fabrication

Each of the three bias circuits was designed using large signal-modeling techniques to exhibit a nominal drain current of 5.0 mA based on a supply voltage of 3.0 V ($V_{dd} = 3.0$). The latter two circuits used a resistor-divider network selected to provide a nominal gate offset of 1.5 V. For the third circuit (Circuit C), FET Q_2 and resistors R_1 and R_2 were selected using large signal methods.

All of these circuits were placed together on the same mask and were fabricated using a MMIC GaAs process. A number of wafers and lots containing all three circuits were fabricated and processed with the intention of significantly varying parametric values for threshold voltage, gate length and current I_{DSS} . Measured mean parametric values for four such wafers are tabulated in Table 1.

Circuits from these wafers were measured, and the results are illustrated in Table 2 and in Figure 6. Each of the circuits exhibited approximately the same nominal quiescent current of 5.3 mA. Performance sensitivity to process can be observed by examining standard deviation in I_{ds} , which is substantially less for Circuit C than the other two. Additional measured parameters are tabulated in Table 2. The performance of Circuit C clearly is superior to the other two. The histograms shown in Figure 6 also illustrate that I_{ds} data for Circuit C tend to be grouped closely around the mean compared to the other two, which are more widely scattered.

Conclusion

The performance of three methods of biasing GaAs MESFET circuits to process variation has been benchmarked. The use of a combination gate and source-resistance feedback method resulted in a significant performance improvement compared to the use of only a source-resistance method. **RF**

Reference

1. J. Michael Golio, ed., *Microwave MESFETs and HEMTs*, Artech House, Norwood, MA, 1991.

About the author

Joe Staudinger received a B.S.E.E. from Kansas State University and an M.S.E.E. from Arizona State University. He has been with Motorola since 1980 working in the areas of large-signal modeling, simulation and circuit design supporting wireless product development. He can be reached at Motorola Semiconductor products sector, MS EL-712, 2100 E. Elliot Road, Tempe, AZ 85284; Tel. 602-413-4456; E-mail ryym71@email.sps.mot.com.

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RF cover story

Integrated test solution emulates real-world environment

By Alex Kim

In wireless communication systems, engineers must take into account various communication channel impairments to adequately compensate with equalization, diversity and error correction. Interference, multipath fading and noise are three impairments that help characterize the wireless channel. These should be used to verify the receiver performance under as realistic a condition as possible. An integrated test solution has been developed that provides the channel impairments called for by cellular, personal communications services (PCS) and satellite communications test specifications. In this article, these impairments are described in detail, as well as their usage and specifications in different wireless standards.

In actual field conditions, interference probably is the most troublesome impairment that degrades the transmitted signal. To emulate interfering signals from either analog phones or from nearby cell sites, continuous-wave (CW) tone generators often are used. It is essential that the phase noise of the interfering signal be low to ensure that the equipment under test is properly evaluated without the uncertainty of the phase-noise effect of the interferer. Especially when testing mobile phones, a CW interfering signal from a base station should be high-quality with low phase noise.

For example, code-division multipleaccess (CDMA) specifications for cellular and PCS require about -105dBm/1.23 MHz of integrated phase noise at 900 kHz offset and -104dBm/1.23 MHz at 1,200 kHz offset, respectively [1]. CDMA specifications test single-tone desensitization and two-tone intermodulation spurious for the receivers in the presence of CW interference. For dual-mode phones, i.e., advanced mobile phone system (AMPS) and CDMA, the phase-noise specifications become even tighter.

Time-division multiple-access (TDMA) specifications call for adjacent and alternate channel selectivity testing. Because the TDMA channel is $\pi/4$ -digital quadra-

ture phase-shift keying (DQPSK) modulated, the integrated test solution for TDMA applications includes a $\pi/4$ -DQPSK modulator at the output of the CW tone generator. (See Figure 1.) Low error vector magnitude (EVM) is required for this modulated signal.

Multipath fading

In a wireless channel, the transmitted signal often is obstructed by natural and man-made structures causing the signal to reach the receiver by more than one path. At the receiver, the direct and indirect path components combine to produce a distorted version of the original transmitted signal. This is called multipath fading, and it can cause significant power losses on the signal when the phase differences among the path components interfere destructively. For example, assuming that there exist two paths of equal amplitude that are delayed so that they produce exactly a 180° (or odd multiples thereof) phase offset, then the paths combine destructively to create deep nulls in the fre-



Figure 1. Adjacent channel Interference for TDMA mobile station.



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quency response of the signal. In the real-world environment, indirect path components exhibit random relative phases. The power envelope can be described by several different statistical distributions, depending on the characteristics of the channel.

Types of fading statistics

1. Rayleigh distribution — This is the most widely used model to characterize the multipath fading channel. Industry test standards for global system for mobile communications (GSM), TDMA (IS-54 and IS-136), CDMA (IS-95 and J STD-008), personal digital cellular (PDC), trans-european trunked radio access (TETRA), APCO-25 and cellular digital packet data (CDPD) among others, specify Rayleigh as the default fading statistic. It is derived mathematically, under the assumption that the amplitude of each path component is the same, and that the phase is random but uniformly distributed. Because the envelope of the sum of two quadrature Gaussian noise signals follows a Rayleigh distribution, implementing a multipath fading emulator based on this model is less complex than with others. This makes it popular and widely used.

2. Nakagami distribution — This is a more general form of Rayleigh fading, where the path component amplitude is assumed to be random, instead of uniform. Intuitively, this may resemble more realistic multipath environments because reflecting objects may consist of a combination of materials such as wood, glass, metal and concrete, each with a different reflection coefficient. Future standards such as universal mobile telephone system (UMTS) and future public land mobile telephone system (FPLMTS) may employ this particular distribution in their standard test plan.

3. Log-normal distribution — Also known as "shadowing," log normal distribution refers to slow, but large-scale, variations of the signal amplitudes over time. This is caused by multipath components that go through a multiplicative process. It is important to realize

that not only the variance, but also the maximum step size in output power level must be specified and controlled for this fading model.

4. Suzuki — This is a combination of log-normal and Rayleigh distributions. Suzuki distribution may be used to describe areas ranging from indoors to outdoors that would encounter deep attenuation as well as many indirect paths.

5. Rician - This is similar to Rayleigh, except it assumes that a line-ofsight (LOS) or strong path exists between the transmitter and the receiver. in addition to the small amplitude scattered paths. Depending on how strong the deterministic path is, compared with the indirect paths, the shape of the distribution changes considerably. The Rician factor, also known as the parameter K, is defined as the ratio between the deterministic signal power and the variance of the scattered paths [3]. As K approaches -----, the strong path component is eliminated, and the Rician distribution becomes Rayleigh. Conversely, if K is large (i.e., amplitude of the



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strong path is large), then the Rician distribution approaches Gaussian [2].

To emulate the multipath environments described above in a laboratory setting, the integrated test solution includes a multipath fading channel emulator. The transmitted signal is shaped by any one of the chosen random fading statistic. Then it is pre-shaped by a finite impulse response (FIR) Doppler spread filter in the frequency domain. By using this spectral filter, accurate time-domain waveforms of Doppler fading can be produced. Depending on the type of the antenna system (e.g., omnidirectional or sectored), the power spectral density of the signal can change. For this reason, Rician provides four types of filters as standard, but the 256-tap FIR filter also is userprogrammable, making it a powerful function.

On the other hand, for some engineers, reproducing the field measurement data in the laboratory setting may be more appealing than depending on statistical distributions. First, by using a channel sounder, impulse response parameters such as path loss, delay and Doppler frequency are measured and recorded. The recorded live data can be "played back" via the multipath fading emulator, enabling full reproduction of the multipath channel response.

Another unique and time-saving function of the multipath fading emulator is its built-in average output power-level setting capability. Power levels of fading signals are difficult to measure because of their fluctuations; therefore, without the power-level setting feature, it may be necessary to average the measurement data over a long period of time. The multipath fading emulator's powerlevel setting accuracy vs. Doppler frequency is 0.1 dB. That accuracy is maintained even if the fading statistic changes. For wideband and spreadspectrum applications, RF bandwidths up to 24 MHz are available.

Additive white Gaussian noise

Another common problem in wireless communication systems is noise, such as white Gaussian noise. All materials produce noise at a power level proportional to the physical temperature of the material. The noise is generated by random vibrations of conducting electrons and by holes in the material. This noise often is referred to as thermal noise. Thermal noise is white and has a Gaussian amplitude distribution.

"White" implies that the power is uniformly distributed over all frequencies, just as white light includes power at all colors. Therefore, the power spectral density of white noise is constant over frequency. This implies that noise power is proportional to bandwidth. "Gaussian" denotes that the voltage amplitude follows a Gaussian probability distribution. According to the centrallimit theorem, if the stochastic variables are independent and equal in significance, then the density of their sum (x = x1 + x2 + ... + xn) tends to a normal (Gaussian) curve as n approaches infinity [4]. Because this type of noise is close in form to the noise found in communication systems, it can be used to

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The NC 500 series drop-in noise modules in TO-8 cans and flat packs for surface mounting are an economical solution for built-in test requirements. These devices contain complete biasing networks and need no external components. Also available are TO-39 packages.

MODEL FREQUENCY RANGE OUTPUT ENR NC 501/15 0.2 MHz - 500 MHz 31 dB NC 502/15 0.2 MHz - 1000 MHz 31 dB 0.2 MHz - 2000 MHz NC 503/15 31 dB NC 506/15 0.2 MHz - 5 GHz 31 dB NC 511/15 0.2 MHz - 500 MHz 51 dB NC 513/15 0.2 MHz - 2 GHz 51 dB

TYPICAL STANDARD MODELS

Broadband Amplified Modules



The NC 1000 series amplified noise modules produce white Gaussian noise from -14 dBm to +13 dBm at frequencies up to 6 GHz. They are designed for coaxial test systems, and are available with several bias voltages and connector options.



The NC 2000 series amplified noise modules are an excellent choice when a high level noise output is desired and the noise source is to be mounted on a circuit board. 24 pin packages are standard; 14 pins are also available.

TYPICAL STANDARD MODELS

OUTPUT

+13 dBm

+13 dBm

FREQUENCY RANGE

10 Hz - 20 kHz

100 Hz- 100 MHz

MODEL

NC 1101A

NC 1107A

TY	TYPICAL STANDARD MODELS						
MODEL	FREQUENCY RANGE	OUTPUT					
NC 2101	100 Hz - 20 kHz	0.15 Vrms					
NC 2105	500 Hz - 10 MHz	0.15 Vrms					
NC 2201	1 MHz – 100 MHz	+5 dBm					
NC 2601	1 MHz – 2 GHz	-5 dBm					



TYPICAL STANDARD MODELS					
MODEL	FREQUENCY RANGE				
NC 302 NC 305 NC 401 NC 406	10 Hz – 3 GHz 10 MHz - 11 GHz 100 MHz – 18 GHz 18 GHz – 110 GHz				

Broadband Precision, Calibrated Coaxial



Noise Com's NC 346 series is designed for precision noise figure measurement applications. These products are available with coaxial or waveguide outputs. For OEM applications, the NC 3200 series provides high performance in a small ruggedized package.

MODEL	FREQUENCY RANGE	OUTPUTEINA					
NC 346A	0.01 GHz – 18 GHz	6 dB					
NC 346B	0.01 GHz - 18 GHz	15 dB					
NC 346C	0.01 GHz - 26.5 GHz	15 dB					
NC 346D	0.01 GHz - 18 GHz	25 dB					
NC 346Ka	0.1 GHz - 40 GHz	15 dB					

Broadband Calibrated Millimeter-wave



The NC 5000 series noise sources feature outstanding stability and convenience in waveguide bands up to 110 GHz.

TYPICAL STANDARD MODELS					
MODEL	FREQUENCY RANGE	WAVEGUIDE			
NC 5142	18 GHz – 26.5 GHz	WR-42			
NC 5128	26 GHz - 40 GHz	WR-28			
NC 5122	33 GHz - 50 GHz	WR-22			
NC 5115	50 GHz - 75 GHz	WR-15			
NC 5110	75 GHz – 110 GHz	WR-10			

Broadband Noise Generators



The NC 6000 and NC 8000 series noise-generating instruments are designed for applications on the test bench or incorporated with other equipment to provide a wide

variety of functions. Each instrument contains a precision noise source, amplification, and step attenuators to provide repeatable symmetrical white Gaussian noise with variable output power.



The new UFX-7000 series noise-generating instruments are extremely easy to use, combining dedicated keys for control of opera-

tions and programming, with a large 4 x 20-character LCD display. Control of output power, filter settings, and attenuator step size for both the noise and the signal (for units with internal combiners) is performed from the front panel or by remotely using the IEEE-488 interface.



TYPICAL STANDARD MODELS					
MODEL	FREQUENCY RANGE	OUTPUT POWER			
UFX-7107	100 Hz-100 MHz	+13 dBm			
UFX-7108	100 Hz - 500 MHz	+10 dBm			
UFX-7110	100 Hz – 1500 MHz	+10 dBm			
UFX-7218	2 GHz - 18 GHz	-20 dBm			
UFX-7909	1 MHz – 300 MHz	+30 dBm			



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Figure 2. A typical base-station setup. The instruments from the integrated test solution described in this article are in gray.

emulate the real-world environment. In general, the random noise is injected into the system, and this type of noise is referred to as additive white Gaussian noise (AWGN).

Because digital communication systems often are characterized by their performance under various signal-tonoise ratios, bit error rate (BER) as a function of bit energy per noise density (Eb/No) is the predominant quality factor for evaluating receiver performance. The BER increases as the Eb/No (or C/N) decreases. The accuracy of BER strongly depends on that of Eb/No. That is, a small change in the Eb/No will cause a large change in the BER. It is critical, therefore, to set the Eb/No accurately with excellent repeatability and stability. Traditionally, though, it has been a manual and cumbersome process to set the desired Eb/No, especially with any meaningful accuracy. For example, CDMA specifications require at least ± 0.2 dB of accuracy, and this can be a daunting task with a manual method.

The integrated test solution automatically provides accurate Eb/No settings (with up to ± 0.1 dB accuracy) to sim-

About the author

Alex Kim is a marketing manager for Noise Com, Paramus, NJ. He has a B.S.E.E. from MIT and an M.S.E.E. from USC. The integrated test solution described is the Wireless Impairment System (WIS) from Noise Com. plify BER measurements. If a user provides the carrier input and enters the bit rate, the desired output power level and the Eb/No ratio, then the instrument automatically provides the combined noise and carrier signal on the output with proper Eb/No setting. Internal broadband noise sources generate high-quality AWGN to emulate the real world as closely as possible.

Conclusion

To properly design and test wireless communications equipment, the channel must be characterized accurately and must be emulated to reflect the conditions in the field. The integrated test solution is tailored to meet general-purpose and standards-specific applications. For TDMA and CDMA applications, the system is ideal for testing fully to the specifications. (See Figure 2.) Other applications such as paging, satellite communications, cable television and digital television also are requiring performance tests under impaired channel conditions. More robust engineering can be performed to alleviate the effects of channel impairments on the wireless communication systems by using proper test solutions. RF

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Figure 3. A typical base-station test system.

RF tutorial

The role of digital signal processors in pager technology

By Xiao-an Wang and Dwane Bell

Pagers and the paging technology have become a large part of the rapidly evolving wireless and mobile communications industry. Advanced paging protocols, including those that support twoway communication, give pager service providers greater capacity to meet the increasing demands for pager coverage and features. These demands present considerable technical challenges to produce products that are competitive both in performance and in cost. Today's integrated circuit (IC) and digital signal processor (DSP) technologies, provide effective means to deal with such challenges. As a result, the market will see more sophisticated, cost-effective pagers with more user-friendly features.

Technology advances are shrinking the differences between pagers and cellular phones, especially among pagers that support two-way protocols. Advanced paging protocols significantly increase channel capacity and add a vast array of functionalities, including two-way communications.

While cellular communications requires high bandwidths and data rates, pagers operate on narrow bandwidths with relatively low data rates. Here are some of the other differences:

• Pagers are primarily receive devices, whereas cellular phones support two-way communications. In two-way paging, however, the user can send a brief response to a received message.

• Paging messages are brief compared to the duration of cellular phone connections. Consequently, the channel capacity of a paging channel (i.e., the number of users allowed) can be hundreds of times that of a cellular channel.

• Because of the short duration of paging messages, a single paging channel usually is adequate for the local coverage area of a service provider. A single pager can be locked to one fixed radio channel, yet the cellular phone has to have the ability to scan all possible channels within the coverage area. The lack of scanning capacity greatly simplifies the receiver because its frequency-synthesizer circuit can be reduced to a minimum.

• Pagers consume less power because one-way pagers do not have a transmitter, and transmission is brief for two-way pagers. In a cellular phone, the transmitter consumes a large amount of power. Moreover, because a

PROTOCOL	DATA RATE	MODULATION	NUMBER OF CHANNELS
POCSAG	512, 1200 and 2400 bps	Binary FSK	
ERMES	6250 bps	Four-level FSK	16
FLEX	1600, 3200 and 6400 bps	Binary FSK for 1600 and 3200 bps, four-level FSK for 3200 and 6400 bps	
ReFLEX	6400 bps FC; 9600 bps RC	Binary or four-level FSK on both channels	
InFLEXion	800, 1600, 6400 and 9600 bps RC; single-sideband (SSB) FC	SSB modulation (for voice) FC, four-level FSK RC	
	KEY: FC - FOR RC - REV FSK - FRI	WARD CHANNEL ERSE CHANNEL EQUENCY SHIFT KEYING	

Table 1. Specifications for the different paging protocols.

pager need not be as responsive as a cellular phone, it can be designed to have a longer "sleep" time. The longer sleep time results in even greater power savings, as well as longer battery life. Current pagers can operate for more than five months on a single AAA battery.

• In contrast to cellular phones and the cellular infrastructure, pagers and the pager infrastructure are less costly to build and maintain.

Paging bands

Paging protocols specify only the modulation methods and the bandwidth of the paging signals. (See Table 1.) Where exactly the paging bands are located is left to service providers and government regulations. Popular paging bands include 138-174 MHz (VHF), 420-470 MHz (UHF), and three bands in the 900 MHz range. Each band is divided into channels. Different bands have different advantages and disadvantages for wireless applications. For example, lower-frequency signals tend to have less path loss and, thus, a wider coverage area. Higher-frequency signals, on the other hand, have a smaller coverage area but better frequency reuse. Frequency reuse involves

the implementation of the same paging band in areas that are far enough apart that the signals in one area will not interfere with the signals in another area.

Paging systems that use the Post Office Code Standardization Advisory Group (POCSAG) of the United Kingdom standard have been ubiquitous in all paging bands, including the relatively new 900 MHz bands. In Europe, the 448 MHz band is widely used for POCSAG systems. Systems based on the European Radio Messaging Systems (ERMES) standard will operate with all 16 of their channels in the 169.4-169.8 MHz band, which has been allocated by all participating countries. Motorola's Flex-based products primarily target the 900 MHz band in the

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Model	• Freq.	LO PWR	Conv. Loss	lsol.(L-R)	Price
	MHz	dBm	dB, Typ.	dB, Typ.	Sea.(1-9)
SKY-5G	2000-5000	+7	6.6	28	14.95
SKY-7G	2000-7000	+7	7.0	28	16.95
SKY-60	2500-6000	+7	6.2	28	14.95
SKY-60LH	2500-6000	+10	6.2	28	16.95
SKY-60MH	2500-6000	+13	6.2	28	17.95
SKY-60H	2500-6000	+17	6.2	28	18.95
SKY-53R	2800-5300	+7	5.7	28	14.95
SKY-53LHR	2800-5300	+10	5.7	28	16.95
SKY-53MHR SKY-53HR • IF: DC-	2800-5300 2800-5300 500MHz n	+13 +17 nin,	5.7 5.7	28 28	17.95 18.95
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Figure 1. Pager functional block diagram.

United States. Theoretically, any protocol can work on any frequency band.

Data transfer rates are determined largely by channel width and by modulation method. Protocols that use fourlevel frequency shift keying (FSK) modulation, such as Flex and ERMES, achieve relatively high data rates (6,250 bps and 6,400 kbps, respectively). The pager must contain a relatively sophisticated demodulation section for the signal to be decoded.

POCSAG

The POCSAG standard has been the most successful standard, possibly because it is nonproprietary and has an extremely simple protocol. In fact, the entire POCSAG document is only five pages long. To date, the POCSAG protocol remains dominant.

POCSAG came about as a de facto standard (being exercised as if legally constituted) by the British Post Office in the late 1970s. It was accepted as an international standard by the Consultative Committee for International Radio (CCIR) in 1981. POCSAG was renamed CCIR Radio Paging Code No. 1 (RPC1), but the old name seems to have prevailed.

A shortcoming of POCSAG is that its data rate is relatively low and, thus, its capacity is low. Its limitations have become more conspicuous as the number of users has grown. Competing protocols, including ERMES and Flex, have been developed to achieve higher capacity.

ERMES

ERMES was developed in the late 1980s and was established as a standard by the European Telecommunications Standards Institute (ETSI). It was recommended by the International Telecommunications Union (ITU) for paging systems intended for international use. Operational ERMES systems have been deployed in France, Germany and Switzerland. Unlike other paging systems, ERMES specifies 16 paging channels. An individual pager is able to receive messages sent on any of the 16 channels, and this requires the pager to have the capacity of scanning and selecting. Such a feature allows the user to roam internationally. As long as there is a roaming agreement between the home and visited networks, subscribers with an ERMES pager can receive messages anywhere they travel.

Flex

In 1994, the Federal Communications Commission (FCC) allocated 3 MHz of the electromagnetic spectrum in the 900 MHz band to narrowband personal communication services (N-PCS): 901-902, 930-931 and 940-941 MHz. The message channels (those on which data and voice are sent to pagers) are allocated in 50 kHz bands, but some of those bands may be subdivided into 25, 12.5 or 6.25 kHz subchannels. The Flex family of protocols-Flex, Reflex, and Inflexion-were designed with the N-PCS bands in mind [1]. Like POCSAG and ERMES, the Flex protocol supports only one-way transmission. Additionally, within the N-PCS bands, the FCC designated eight 12.5 kHz response channels, which allow pagers to transmit messages. Reflex and Inflexion support the use of message and response-channel pairs to enable two-way paging. Reflex supports the sending and receiving of alphanumeric messages and data. Inflexion-based pagers receive voice messages and transmit acknowledgement responses. Both InFLEXion and Reflex use the concept of location-specific transmission, which provides the frequency reuse feature so the paging capacity can be increased further across the infrastructure.

Because a majority of paging service providers have a license for only a single 50 kHz channel, increased capacity has to be achieved by more efficient channel use. Within a 50 kHz band, only two Flex channels can be accommodated. However, the relatively large bandwidth has spurred the development of Reflex50, a Reflex-based protocol that enables a data rate of 25,600 bps on a 50 kHz channel.

Transmission modes

A significant advantage of ERMES and Flex is battery saving caused by their synchronous transmission characteristics. A synchronous protocol allows the pager to switch on periodically (e.g., every couple of minutes) and check to see whether a message is being sent. The pager's controller circuitry can place unused peripherals into various levels of "sleep," depending on whether the unit is checking for messages, processing received data, interacting with the user, sending responses or being inactive. A POCSAG pager uses an asynchronous protocol, so it must spend more time with its circuitry in active mode.

Pager receiver design

Figure 1 is a functional block diagram of a pager receiver. The RF modulator downconverts the RF input signal to baseband. Flex and ERMES pagers typically require multistage downconversion, whereas POCSAG pagers can use direct conversion. After the baseband signal is converted to a digital signal, it is processed by the baseband demodulation function to produce a bit stream of the received data.

The data bits from the demodulator are considered to be the raw data, possibly corrupted by noise during transmission. It is the decoder's task to recover the message from the raw bits. This is accomplished through the following steps.

• Frame synchronization — The decoder aligns its receive buffer to the frames in the received bit stream. Generally, the bit stream is divided into 32-bit frames by protocols. For MICROWAVE & RF Division Microwave diodes Ferrite devices Microvave modules Waveguide components

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	6	TE5100	6	7.50	60	22.5	-	-		3	2.0	90	3300//0	
	8	TE5110	6	7.50	60	15.0	80	20.0		3	2.0	100	3300//0	
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	6	TE5240	6	6.50	60	22.5	-	-		4	2.0	90	1400//0	(49)89.51.640
-	8	TE5250	6	6.50 7.50	60 15	17.5	80	22.5		4	2.0	100	1400//0	(Fax)
	4	TE5270	3	7.50	30	25.0	-		1212	3	2.0	70	1600//0	(49)89.51.64.194
	6	TE5280	6	7.50	60	25.0	-	-		4	2.0	90	1600//0	
	8	TE5290 TE5300	63	7.50	60 15	50.0	- 80	25.0		4 2	2.0	45	3000//0	1 520 5740
	4	TE5310	3	15.0	30	45.0				3	2.0	60	3000//-1	A DECK LIN
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Figure 2. Scope of DSP use in pager receivers.

ERMES and Flex, deinterleaving also is performed.

• Information retrieval — The framed raw data are sent to the error control decoder to extract the address data, ID data and message data. In the process, errors in the raw data bits get corrected by the decoder so that the decoded data will have an extremely low bit error rate (BER).

• Address match — The decoder examines the address field in the decoded frame to determine whether the message is for the particular pager. If not, the decoder informs the controller, and the controller shuts off major receiver parts to conserve power.

The controller interprets the corrected message from the decoder in its intended form (numeric, alphanumeric or voice) and delivers it to the user by either liquid crystal display (LCD) or by speaker. It also handles the unit's power management by switching the pager's circuitry on and off as needed.

The DSP in lowand high-tier pagers

The pager market can be divided into two tiers: low-tier and high-tier. To a large extent, the tier will determine how a DSP configuration will work. Low-tier pagers include POCSAG pagers and some Flex numeric pagers. This tier can be characterized by mature, simple technology.

POCSAG receivers have simple but robust structures. POCSAG-based numeric pagers can be made as compact as a pen or as thin as a wristwatch or a credit card.

The low-tier pager has rendered DSP advantages irrelevant. For example, the simple POCSAG receiver structure minimizes the advantage of a higher degree of integration. Proven and wellestablished POCSAG decoder chips make the new round of DSP development unnecessary. The modulation scheme is handled adequately by analog circuits without the need for digital filtering. The core operations of the POCSAG pagers are binary and bitoriented. For a DSP product, most of the special modules of a DSP chip, such as the hardware multiplier and the filtering structure, would remain inactive during those operations.

For high-tier pagers, including those based on ERMES and on most of the Flex family, a DSP-based pager shows great potential and is indispensable for some applications. For example, Inflexion- and Reflex-based pagers operate on densely packed channels. There are seven 6.25 kHz voice channels in a 50 kHz channel for Inflexion. In such cases, digital filtering appears to be the only feasible choice for suppressing adjacent interchannel interference because the transition band and out-of-band attenuation of a digital filter can be designed to meet the stringent specifications.

The complexity of the high-tier pagers requires more components in receiver design. This makes the cost and power consumption of DSP chips a less serious problem. For alphanumeric pagers, the display takes up a considerable size, which makes the size of a DSP chip a lesser concern. High-tier pagers also require the implementation of more processing functions. Thus, the advantage of a high degree of integration of the DSP product can be significant. For two-way pagers, a DSP can perform most of the transmission functions, including the sophisticated Reed-Solomon encoding.

Higher integration within the DSP also helps to reduce the power consumption. Although an applicationspecific integrated circuit (ASIC) decoder chip set consumes less power, the power consumption of the DSP chip can be made comparable to the set of components it replaces.

There are other advantages to having a DSP in high-tier pagers. For example, a DSP is a natural candidate for voice signal-processing in voice pagers. To further increase the channel capacity, 16-quadrature amplitude modulation (QAM) or even 64-QAM is expected to be used in the future. Again, a DSP is most suitable to demodulate, and possibly, to equalize such signals.

Use of the DSP in pager designs

Figure 2 shows that a DSP can implement most of the pager's receiver operations, whereas an alternative would require several devices to cover the same functions. For two-way pagers, most transmission functions, including data generation, encoding, and pulse shaping, also can be implemented on the DSP. In contrast to an ASIC-based chip set, a DSP is easy to program, debug and test. This significantly shortens the development period and delivers a design that pager manufacturers can bring to market quickly.

Other DSP characteristics include:

• Easy upgradeability — Paging protocols keep changing and keep being updated to meet the ever-increasing demand for capacity and new features. Because a DSP is programmable, protocol changes can be accommodated by modifying DSP programs.

 Plug-and-play nature — A DSP chip with built-in analog-to-digital (A/D) and digital-to-analog (D/A) converters and controller functions easily can be interfaced with the analog signal from the RF unit output and with the control inputs of the display. As a comparison, current ASIC-based solutions require preprocessing to convert the analog signal to digital form. In addition, they require postprocessing by a microcontroller. Because pager IC manufacturers typically do not provide the microcontroller, pager manufacturers are left responsible for choosing and programming it.

In some applications, an ASIC proves superior to a DSP. In particular,

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Figure 3. Block diagram of the DSP.

when ASIC chip sets are tailored specifically to a pager application, they can be both more cost-effective and more power-efficient. The better choice between an ASIC-based solution and a DSP-based solution usually will depend on which pager protocol is being followed.

DSP-based solution

A DSP specifically has been designed to provide versatile paging. Both the DSP and its paging software library are designed to meet current paging protocols and to support evolving paging protocols. A 20 millions of instructions per second (MIPS) mixed-signal device core, the DSP contains 24K 16-bit words of read-only memory (ROM), 2K 16-bit words of dual-port, randomaccess memory (RAM) and several peripheral blocks. The core contains a data arithmetic unit, memory addressing units and cache. The device is illustrated in Figure 3.

To achieve power savings and costeffectiveness, the DSP integrates the digital circuitry with A/D and D/A converters, a clock synthesizer, a memory controller, an interrupt controller and serial input-output (I/O) controllers. The integration results in the functionality usually found only across an entire chip set. Microcontroller-type functions are implemented through the five timers and the four 8-bit ports. The serial peripheral interface is designed to drive an alphanumeric display.

To further reduce device cost and power dissipation, the clock synthesizer was designed to be driven by a lowspeed (32 kHz or 38.4 kHz) external crystal. The crystal drives an on-chip phase-locked loop (PLL) that generates clocks required for the internal functions. Through on-chip power management, peripherals can be switched off when they are not in use. Under a 2.7 V supply, the device runs

at 0.9 mA/MIPS in active mode. In full sleep mode, only 18 µA is consumed.

For current paging solutions, the DSP runs at less than 10 MIPS—less than half of its capacity. This leaves plenty of room for designers to add new features and functions. Alternatively, the clock frequency can be lowered to achieve further power savings.

Protocol independence also makes the DSP a platform that nicely enables pager designs. Programmability in the system architecture is an important factor in pager technology because the signal-processing requirements are dependent upon the protocol, and it is not yet clear what protocols will be dominant in many developed and undeveloped markets. This DSP was created for wireless messaging that can support protocols as the markets evolve.

Market conditions demand that signal-processing supports rapid application development and easy upgrades to existing designs. Programmability allows designs to be changed and new protocols to be implemented through software updates.

Through placing on-chip flash memory where the ROM normally is found, a "flash version" allows developers to load and to debug application software on the spot, instead of waiting several weeks for the DSP to be ROMcoded with the software.

In addition to costs reduced through programmability as well as a high degree of integration, further cost reductions are achieved through design innovations that enable the DSP, which is a mixed-signal device, to be manufactured entirely in digital complementary metal oxide semiconductor (CMOS) technology. No additional masks are required for the inclusion of analog circuitry.

Conclusion

The role of a DSP in paging designs is largely based upon the protocol followed. For pagers designed to support a relatively simple protocol such as POCSAG, an ASIC-based implementation generally is more cost-effective. But for designs based on ERMES and on the Flex family of protocols, a DSPbased solution may be the only viable option because of the signal processing required to detect the information in the received signal. A DSPbased pager also gives the designer the ability to tailor a pager design to meet evolving protocols simply through updating the DSP software. A DSP that contains such on-chip functionality as controller tasks and clock synthesis can prove to be even more effective. RF

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The DSPs described in this article are the DSP1615 and the FlashDSP 1615, both available from Lucent Technologies Microelectronics Group, Allentown, PA.



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RF distortion

Reducing IM distortion in CDMA cellular telephones

By Dick Bain

Code-division multiple-access (CDMA) spread-spectrum technology enables more cellular users to coexist in a given segment of the allocated cellular frequency band. This will be a boon to those carriers struggling with overburdened analog cellular systems in highdensity markets such as the Los Angeles area. Unfortunately, a problem has appeared in high-density markets where the CDMA systems have been tested. The gremlin is interference caused by intermodulation distortion (IMD) products generated in a CDMA receiver from multiple off-channel analog signals. What are these products, and how are they generated?

IMD products are generated when two or more signals pass through an active or inactive device in a receiver or transmitter. The most troublesome products are of two types: two-tone (two signal), third-order products and threetone (three-signal) IMD products. Figure 1 shows the third-order, twotone IMD products and the two signals from which they derive. The following formula describes how the third-order products are generated:

$$f_{IM} = 2f_1 - f_2$$
 and $2f_2 - f_1$.

The three-signal IMD products are generated as follows:

$$f_{IM} = f_1 + f_2 - f_3$$

= f_1 + f_3 - f_2
= f_2 + f_3 - f_1

Three tones and their products are shown in Figure 2. The third product is not visible because it is the same frequency as f_2 . There are other, higherorder products, such as 5th order and 7th order, but these generally are at a much lower level than the third-order products and therefore often can be ignored. A helpful tutorial on IM distortion appeared in the February 1996 *RF Design* [1], and a paper discussing the IMD problem in CDMA systems was presented at the 1996 IEEE Vehicular Technology Conference [2].

Which devices in a receiver generate IMD products? When multiple signals pass through any device, mixing action occurs because of the non-linearities of the device. No device has perfect linearity; even a passive device such as a type N connector will generate IMD products, though passive devices generate only small levels of IMD products compared to most active devices. The level of IMD products a device will generate can be characterized by the device's intercept point. Figure 3 is a graphical representation of the third-order intercept point (IP₃) of a device. The higher the intercept point, the lower the level of IMD products generated for a given level of input tones. So why not simply use high intercept point devices to solve IMD problems in CDMA phones? The drawback is that a higher IP₃ generally means higher supply current. To raise the IP₃ of an amplifier by 3 dB, for instance, the collector current generally would have to be doubled. It is possible



Figure 2. Third-order, three-tone IM tones and products.





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Figure 4. A 20 dB, switched front-end attenuator.

Figure 5. Fixed attenuator operation.

to use some type of distortion-canceling scheme using feedback or feed-forward techniques to achieve higher IP_3 without increasing device current but, unfortunately, distortion-canceling techniques involve significant amounts of additional circuitry, added cost and additional board space. Because the phone operates on battery power, increasing device current shortens the operating time of the phone before the battery needs to be recharged. What else can we do to treat this problem?

Raising the CDMA base station power seems like another logical solution. Unfortunately, CDMA and analog are often collocated at a base station and share the same power amplifier. Because the total power from the amplifier is constant, raising the CDMA power means lowering the power in the analog signals and reducing the reliability of communications for the analog cellular phone customers. Fortunately, there is an answer that avoids the problems of the previously referenced solutions. Sacrifice some surplus signal-to-noise ratio to reduce IM levels.

The following formula indicates how much IM will be generated by a given device with a particular level of input signals:

IMD = 3S - 2IP

where:

- S = the level of each tone applied to the device in dBm
- $IP = the device's IP_3 in dBm$

Note that if the tone level is dropped by 1 dB, the level of each IMD product drops by 3 dB. Because this is so, if the input signals are attenuated by 1 dB, the signal to IMD ratio will improve by 2 dB. When the receiver is operating above the level of its minimum sensitivity, it is possible to sacrifice some signal-to-noise ratio to increase the third-order intercept point and thereby reduce the level of IMD products generated. This can be done by switching an attenuator in series with the front end of the receiver, preferably before the first active device, to achieve maximum reduction of IM distortion products.

Fixed attenuator solution

A fixed attenuator can be switched in or out at a selected RF input level to reduce IM distortion at signal levels above threshold. This can be accomplished with a comparator that compares the level of the receiver's automatic gain control (AGC) voltage with a settable reference voltage as shown in Figure 4. Figure 5 shows how the signal level would change if a 20 dB attenuator were switched in series with the front end of a receiver. Notice that the attenuator must be switched in at an input signal level that is higher than the level at which it is switched out. This signal level increment, known as hysterisis, needs to be incorporated to avoid chattering, which otherwise would occur at the threshold point of the attenuator. Without the hysterisis, a signal at threshold level could cause the attenuator to switch in and out rapidly and repeatedly because of small fluctuations of the AGC or received signal strength indication (RSSI) input to the comparator. (Although RSSI originally was intended to drive a signal

strength indicator in an FM receiver, in a dual-mode CDMA receiver, it can be used as an AGC voltage in the CDMA mode to control the gain of an amplifier.) In the case shown in Figure 5, the attenuator operates at an input level of -70 dBm and drops out at -75 dBm input. The pull in point of the attenuator is set by the amount of hysterisis needed and the drop out point required. The drop out point is determined by the threshold sensitivity of the receiver. For the CDMA cellular receiver, it is necessary to have the attenuator drop out at -75 dBm, so the signal will not drop below -95 dBm, and so a signalto-noise ratio of at least 9 dB above minimum sensitivity will be maintained. The present CDMA receiver sensitivity recommended by the **Telecommunica-tions** Industry Association (TIA) document IS-98A is -104 dBm.

When the fixed attenuator is in the circuit, the third-order IMD products will drop by 60 dB, and the signal-to-IMD ratio will improve by 40 dB. Unfortunately, because the attenuator is disengaged for signal levels below -75 dBm, no IMD relief is available, and call drop outs may be a problem. Fortunately, there is another attenuator solution that offers IMD product reduction at significantly lower receiver RF input levels.

Variable attenuator solution

Positive intrinsic negative (PIN) diodes are devices that can be characterized as resistors with an RF resistance that decreases as the current through them increases. Although these devices make excellent switches,

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0.01-200	AU-1447	56	0.5	2.0:1	1.2	1.2	1.2	12	\$325
0.01-500	AU-1310	30	0.5	2.0:1	1.3	1.4	1.5	8	\$325
0.01-500	AU-1332	45	0.5	2.0:1	1.3	1.4	1.5	10	\$350
0.01-1000	AM-1300	27	0.75	2.0:1	1.4	1.6	1.8	8	\$350
0.01-1000	AM-1431	35	0.75	2.0:1	1.4	1.6	1.8	10	\$375
0.02-1000	AM-1551	38	1.0	2.0:1	1.4	1.6	1.8	16	\$375
1-100	AU-3A-0110	53	0.5	2.0:1	1.2	1.2	1.2	12	\$300
1-200	AU-1464	35	0.5	2.0:1	1.2	1.2	1.2	6	\$275
1-200	AU-1494	56	0.5	2.0:1	1.2	1.2	1.2	12	\$300
1-500	AU-2A-0150	30	0.5	2.0:1	1.3	1.4	1.5	8	\$275
1-500	AU-3A-0150	45	0.5	2.0:1	1.3	1.4	1.5	10	\$300
1-500	AU-4A-0150	60	0.5	2.0:1	1.3	1.4	1.5	10	\$325
1-1000	AM-2A-00011	0 27	0.75	2.0:1	1.4	1.6	1.8	8	\$300
1-1000	AM-3A-00011	0 35	0.75	2.0:1	1.4	1.6	1.8	9	\$325
1-1000	AM-4A-00011	0 52	1.0	2.0:1	1.4	1.6	1.8	9	\$350
5-300	AU-1021	24	0.5	2.0:1	2.4	2.5	2.7	20	\$275
5-300	AU-1525	61	0.5	2.0:1	1.2	1.2	1.3	20	\$350
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100-2000	AM-1526	9	1.0	2.0:1	4.5	4.0	4.2	20	\$350
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Figure 7. Series PIN diode attenuator.

Figure 6. Shunt PIN diode attenuator.

they also can be used as current controlled RF attenuators. This capability has been harnessed to reduce IMD products in a CDMA cellular telephone and thereby increase communications reliability by significantly reducing dropped calls. Figures 6 and 7 show two ways to incorporate a PIN diode attenuator in a cellular phone receiver. We chose the shunt configuration for three reasons:

1. The shunt configuration requires fewer parts.

2. The stray inductance of the device is easily resonated out with a series capacitor. With the parasitic inductance resonated out, the measured attenuation of the shunt attenuator was a nominal 20 dB. A series attenuator requires a parallel inductor (L1 in Figure 7) to resonate the parasitic capacity of the diode to provide a high resistance when the diode current is minimum. A 1% tolerance part that is parallel-resonant with the stray capacitance of the diode is needed to achieve the full attenuation of the series PIN diode attenuator. In the case of the shunt attenuator, a 1% tolerance series

capacitor is needed to resonate with the stray inductance of the PIN diode. Unfortunately, an inductor with a 1% tolerance is much more expensive than a capacitor with a 1% tolerance, and the procurement process of such inductors would have to include a long lead time—if they could be obtained at all.

3. The shunt PIN diode attenuation increases rapidly at the beginning of its attenuation curve. In the case of the series attenuator, the greatest attenuation change occurs at the end of its attenuation range because the diode current is maximum at minimum attenuation, and attenuation increases as the current through the diode is decreased. The rapid change of attenuation vs. diode current at small diode currents of the shunt attenuator has important consequences.

Figure 8 shows the measured attenuation vs. control voltage for a shunt attenuator. This is the voltage applied to a resistor in series with the diode. Notice the rapid increase in attenuation at levels between 0.5 and 1.0 VDC, which corresponds to about -95 dBm to -75 dBm. This means that there will be significant reduction of IM products even at -90 dBm input to the receiver, as opposed to the fixed attenuator case, where the attenuator offers no IM reduction until it is switched in the circuit at -70 dBm. Figure 9 shows the maximum tolerable tone levels during a two-tone IM test with the shunt attenuator active and inactive. The criteria for the CDMA IM test is a frame error rate (analogous to bit error rate) not exceeding 1% at the specified tone level. The area between the curve measured with the attenuator deactivated and the curve measured with the attenuator activated represents the improvement in receiver IM performance. Field tests show this improvement eliminates almost all dropped calls in a busy cellular market such as the Los Angeles area during times of peak use.

To take advantage of the full benefit of the PIN diode attenuator, it was necessary to temperature-compensate the RSSI voltage of the receiver with a temperature sensor integrated circuit (IC) and several sections of an IC as amplifiers and summers. This reduced the variation in the turn-on point of the



Figure 8. Attenuation vs. voltage.







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This PIN diode attenuator remedy for the IMD problems encountered in highdensity markets, along with the other advantages of CDMA cellular systems, brings the CDMA system one step closer to providing badly needed additional capacity to supplement existing analog cellular systems.

Acknowledgements

I acknowledge Bob Lyall's contributions to the design and testing of the PIN diode attenuator and Pat Maresca's design and testing of the temperature compensation circuit. A patent has been applied for that covers the use of a variable PIN diode attenuator to reduce IM distortion as described in this article.

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About the author

Dick Bain, an RF staff engineer, conducts CDMA and PCS receiver design and support work at OKI Telecom. He has previously worked as an RF engineer at Aritech Moose, the ECI division of E-Systems, and at Magnavox. He received a B.S.E.E. from Indiana Institute of Technology. He holds an amateur Extra class license, N4RB. Several of his articles have appeared previously in *RF Design*. He can be reached at OKI Telecom, 437 Old Peachtree Road, Suwanee, GA. Tel. 770-995-9800, ext. 1402.



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A dual-channel wideband high-frequency (HF) receiver, model 9640, features an output frequency range of 1–11 MHz, a 4 MHz bandwidth, 53 dB nominal gain and 2:1 maximum voltage standing wave ratio (VSWR). Interad Info/card 175

Chip makes speech more intelligible

A smart preamplifier system-on-a-chip features variable compression and automatic noise gating to give microphone-level signals as high as 20 kHz a higher degree of intelligibility. With a single, user-selectable, external resistor, the SSM2166's compression ratio can be customized to produce a steady, undistorted audio output level even though signal inputs vary. The SSM2166 also limits high levels, amplifies low levels, and features signal compression, adjustable noise gating, automatic signal limiting and 5 V singlesupply operation. It is priced at \$1.50 in quantities of 10,000.

Analog Devices Info/card 176

High-speed 2.4 GHz wireless bridge

The BR2040-EE highspeed wireless bridge is the next addition in a series of 2.4 GHz direct-sequence spread-spectrum (DSSS) bridges. The bridge can connect Ethernet networks at a data speed of 4 Mbps as far as six miles apart using a parabolic grid antenna in line-of-sight applications. The bridge operates in the 2.4 GHz industrial, scientific and medical (ISM) frequency band at an output level of as much as 100 mW so as to limit the effective isotropic radiated power (EIRP) to the 4 W Federal Communications Commission (FCC) maximum

Aironet Wireless Communications Info/card 177



Crystal offers highfrequency stability

The ECCM5 microprocessor crystal is a compact ($6 \times 3.5 \times 1$ millimeters) ceramic surface-mount device offering the high degree of frequency stability required by advanced communication applications. The ECCM5 series is available at a frequency range of 10–150 MHz and can sustain ±10 ppm tolerance and ±5 ppm

stability. It is designed for use in wireless, RF, microwave, telecom and satellite applications. Ecliptek Info/card 178

OCXOs at 10 and 26 MHz

Oven-controlled crystal oscillators (OCXO) models XO5026-003 at 10 MHz and XO5026-004 at 26 MHz both feature -155 dBc/Hz phase-noise performance at 10 kHz offset. They also feature less than $\pm 4 \times 10^{-10}$ per day aging, complementary metal oxide semiconductor (CMOS) output and a unit price of \$220 at quantities greater than 1,000.

Piezo Technology Info/card 179

Miniature surface-mount clocks

Models 042 and 342 are surfacemount quartz crystal clock oscillators designed for use in a variety of commercial applications, including personal communications services (PCS) base stations, cellular base stations, synthesizers, digital switching, test equipment and avionics. Both clocks cover a wide frequency range of 1–85 MHz. Model 042 has a 5 V supply. Model 342 has a 3.3 V supply. Both clocks are transistor-transistor logic (TTL) and analog complementary metal oxide semiconductor (ACMOS) compatible. **Oak Frequency Control Group Info/card 180**

VCOs tune from 1,930–1,990 MHz

The VCO190-1960T and VCO191-1960U both are voltage-controlled oscillators (VCOs) that tune from 1,930–1,990 MHz. The 190 has a tuning voltage of 2.0–3.7 V typically, draws 10.5 mA (typical) from a 5 V supply and has a typical phase noise at 50 kHz offset of -116 dBc/Hz. The 191 has a tuning voltage of 0.9–2.3 V typically, draws 6.5 mA (typical) from a 3 V supply and has a typical phase noise at 50 kHz offset of -114 dBc/Hz. Vari-L Info/card 181

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Synthesizers deliver -100 to 10 dBm amplitude

The series 50000A VXIbus microwave synthesizers give users the ability to generate, modulate, level and attenuate RF output signals from 10 MHz to 20 GHz. The synthesizers use a twoloop indirect synthesis design with a fundamental YIG-tuned output oscillator phase-locked through a reference loop to a crystal-controlled time base to produce frequency accuracy and stability, frequency resolution and spectral purity. The result is frequency stability better than 3 Hz per GHz per day, frequency resolution of 1 Hz, harmonics



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<=-50 dBc from 2-20 GHz and single sideband (SSB) phase noise from 2-20 GHz of -97 or less at a 100 kHz offset. The Series 50000A microwave synthesizers are available in 11 models with prices starting at \$20,750. **Giga-tronics Info/card 182**

Sweep system has multiuser capability

The 3HRV headend reverse sweep receiver simultaneously can perform 10 reverse sweeps and helps to eliminate the effect of ingress on the measurement. The 3HRV can stand alone for reverse alignment only or can be used in conjunction with the 3ST transmitter to provide full forward and reverse sweep alignment. The system also features an in-service signal analyzer for measuring carrier-to-noise and hum, a reverse noise and ingress spectrum display and a digital QAM carrier-level measurement option. Wavetek

Info/card 183

CDMA AWGN generator achieves ±0.1 dB accuracy

The UFX-BER series of code-division multiple-access (CDMA) mobile- and base-station testers generates additive white Gaussian noise (AWGN) and automatically sets accurate C/N (Eb/No) ratios. This greatly reduces frame error rate (FER) test time in laboratory and production environments. The UFX-BER series features ±0.2 dB C/N accuracy with an optional ±0.1 dB and a typical crest factor of 18 dB. **Noise-Com Info/card 184**

Accelerometer calibration at ultra-low frequencies

The MB WIN475 vibration transducer calibration system with the lowfrequency option makes it possible to have less than 1.25% system accuracy from 1–10,000 Hz. The MB WIN475 allows users to maintain a 4:1 ratio when calibrating 5% devices to 1 Hz. **MB Dynamics Info/card 185**

One-box system simplifies testing battery life

The 66312A and 66332A one-box, DC power supply functions both as a power

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INFO/CARD 47

source and as a dynamic-measurement subsystem to assess battery-operating times quickly and accurately. Designed to simplify the testing of batteryoperating time for cellular phones, mobile radios and other digital wireless communication products, the 66312A half-rack 40 W DC source and the 66332A full-rack 100 W source are priced at \$1,695 and \$2,095 respectively. Hewlett Packard Info/card 186

Signal generator guarantees output power of 10 dBm

A compact, programmable microwave signal generator, model 8003, covers 2–20 GHz in 1 MHz increments with a guaranteed output power of 10 dBm. It features a -90 dBc typical phase noise at a 20 kHz offset from the carrier and spurious output typically less than -60 dBc. The 8003 requires less than 30 WAC power and is priced at \$8,995.

April Instrument Info/card 187

Signal source provides atomic clock accuracy

Model 2955AR rubidium standard with synthesized output has a directdigital synthesizer output that is 32 bit programmable from 10 Hz to 4 MHz. It also has fixed outputs at 1 and 10 MHz. The synthesized output has spectral purity with typically less than -135 dBc phase noise at 1 kHz offset and long-term stability equal to the rubidium atomic clock. The 2955AR can be set to standard frequencies and also can be used as a master oscillator in laboratories and in ground stations as well as for test and calibration. The system is priced at \$4,295.

Novatech Instruments Info/card 188

AMPLIFIERS

Power amplifier meets PCS and PHS requirements

Model CMM1333 is a surface-mount SO-8 packaged digital power amplifier designed for personal communications services (PCS) and personal handyphone systems (PHS) operating in the 1.85–1.91 GHz frequency band. The amplifier features 30 dBm time-


division multiple-access (TDMA) digital output power from a standard 5 V supply with 40% efficiency and 32 dB gain. The amplifier's high gain and efficiency eliminate the need to require a driver amplifier within the handset circuitry. The CMM1333 is priced at \$20 in quantities of 1,000. **Celeritek**

Info/card 189

Power amplifier meets high-linearity requirements

The ADCA-896-40 10 W linear cellular power amplifier is designed to meet the high-linearity requirements imposed by most multicarrier and digital transmission systems. It includes an internal isolator to protect against high voltage standing wave ratio (VSWR) and to ensure stable performance under any load condition. The ADCA-896-40 operates over the 869–894 MHz frequency range. AdComm

Info/card 190

Power amplifier operates from 30–100 MHz

Model 100-30-120-35-E3 class AB power amplifier is a compact amplifier (6" \times 2" \times 1") featuring high-efficiency and low-harmonic output. It also features a gain of 40 dB typical, 50 Ω input and output impedance, a 30–100 MHz operating range and a saturated output power of 120 W. The unit is priced at \$5,950. LCF Enterprises

Info/card 191

RF amplifier provides high output power

The MHW2821-1 and MHW2821-2

RF power amplifiers operate in the 806–950 MHz frequency range and are designed for 12.5 V UHF applications. The MHW2821-1 requires an RF input power of \leq 250 mW and an RF output power of 20 W. MHW2821-2 requires an RF input power of \leq 300 mW and an RF output power of 18 W. Man-

ufactured using laterally diffused metal oxide silicon (LDMOS), the amplifiers feature 50 Ω input and output impedances, stability, ruggedness and low harmonics. Both models are priced at \$42.90 in low volumes. **Motorola Semiconductor Info/card 192**

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Technology blocks offer increased integration

Silicon Systems, a Texas Instruments company, has a custom IC program that offers design teams access to technology blocks for implementing advanced, high-performance, digital, application-specific integrated circuits (ASICs) for mass storage applications. The technology blocks include disk formatters, headerless disk formatters, error detection and correction, buffer management, host interfaces and microprocessor interfaces, that ensure proper operation between blocks. The technology blocks speed development and integration and facilitate final device testing.

Silicon Systems Info/Card 153

Modem algorithms available for DSP cores

VoCal's library of data modulation, fax modulation, speech coders and other telephony standards, including V.34 Annex 12 (33,600 bps) and fullduplex speakerphone, are available for the Analog Devices ADSP-2100 digital signal processor (DSP) core. Original equipment manufacturers (OEMs) can license the core from Analog Devices or from Mentor Graphics. The software library will allow users to embed the DSP architecture, supported by algorithm libraries and hardware and software development tools to produce communication and multimedia products. **Analog Devices** Info/Card 154

Antenna analysis software enables viewing capabilities

NEC-Win Basic provides an interface to the standard NEC-2 core as well as the capability to view antenna structures and to produce radiation and surface-pattern plots. NEC-Win Pro extends those capabilities. Features include: NEC-2 support with graphical entry for all commands, including surface patches; an antenna geometry viewer under Windows, with capability to view currents, sources, loads and transmission lines in addition to the viewing features found in NEC-Win Basic; wire identification within the NEC-Win Pro viewer that allows the user to click on a wire and have the input file highlight the wire; a 3D antenna pattern viewer under Windows that enables the user to view the pattern and the antenna simultaneously with independent zoom control; expanded polar plotting that includes electric fields in addition to save features; rectangular plotting capability for viewing voltage standing wave ratio (VSWR), currents and radiation patterns; Smith charts for examining VSWR vs. frequency; and integrated NEC-Win Basic capability with spreadsheet operations.

NEC-Win Pro comes on four disks with a three-volume user manual. Paragon Info/Card 155

Design process simplified

MicroSim Schematics version 6.3 software for electronic design automation (EDA) includes enhancements that apply to the company's range of products from schematic entry through printedcircuit-board layout. Software capabilities include a graphical part browser, error traceback, a symbol creation wizard for improved schematic entry, a goal functions wizard and expanded libraries for enhanced simulation.

The graphical part browser lets the designer select a part from the 40,000 plus symbol library by name, number or description. Error traceback helps the user to find the source of design entry errors. A pop-up window alerts designers to any errors during netlisting, packaging and other operations. The symbol creation wizard provides a step-by-step process to define symbol shapes and adjust them as pins are added. Multiple pins may be added, named and numbered sequentially.

MicroSim's simulation products, MicroSim PSpice and MicroSim PSpice A/D contain goal functions, such as rise-time and bandwidth, that extract performance data from waveforms. The release of both simulation programs provides a model for a power semiconductor device, the insulated gate bipolar transistor (IGBT), which provides more than 150 IGBT models from which to create custom circuits. **MicroSim**

Info/Card 156

Software addresses spectrum management

Phasor Design's Splash predicts the detailed spectral occupancy of transmission by a detailed mathematical modeling of the modulation process. The software simulates the key transmitter characteristics that determine spectrum use. Baseband signals are generated, shaped and processed to accurately model reality. For FM systems, the non-linear modulation process is simulated mathematically, allowing spectrum expansion to be examined. Splash is a Microsoft Windows application and runs on an IBM or compatible 486 or above.

Phasor Design Info/Card 157

VXI instruments provide scaleable test systems

The VXI plug and play-compliant line of multifunction VXI-based multifunction data acquisition (DAQ) instrument modules, from National Instruments, delivers scaleable test to users who have developed applications using the company's DAQ products for PC and XT, AT, EISA, PCI, NuBus or PCMCIA. Because the modules use NI-DAQ driver software, users can run their applications on the VXI-based modules with no software rewrite.

The R&D engineer can test initial designs using a PC-based system; the test engineer can reuse this software with a VXI system for production; the service technician can again reuse the same software with a lap-top computer and the company's PCMCIA-based DAQ interfaces.

National Instruments Info/Card 158

Software and hardware aid Lode DSP core

A software and hardware development platform for the Lode digital signal processor (DSP) core is available from TCSI. Lode is a 16-bit DSP designed for high performance in digital cellular, speech and voice communications applications.

The suite of tools includes an assembler, linker, simulator and hardware development platform. The software components allow the DSP programmer to develop and verify application software. The hardware platform enables a DSP programmer to analyze the efficiency of an application before implementation. TCSI

Info/Card 159

Handbook combines resistor theory, application

The Resistor Handbook by Cletus J. Kaiser combines resistor theory with practical circuit application information. This book complements the author's The Capacitor Handbook and The Inductor Handbook. The first chapter covers the fundamentals of all resistors followed by chapters on composition, film, wirewound and nonwirewound types of resistors. Later chapters cover thermistors, shunts, current shunts and current sensors. A glossry, symbols and equations, resistor selection guidelines and index also are included. The 100-page book costs \$15.95 plus \$4 shipping and handling. **CJ** Publishing

Info/Card 160

Designer's guide available

Mini-Circuits' 180-page RF/IFDesigner's Guide contains practical articles, a glossary of terms, environmental and reliability test procedures, answers to frequently asked questions about surface-mount technology and specifications and prices for the company's signal-processing components. The guide is free and may be obtained by mail, fax, phone or E-mail. Mini-Circuits Info/Card 161

Catalog includes test instruments and tools

The fall catalog from Contact East includes test instruments and tools for those involved in design, R&D, testing, quality control and management. Product highlights include oscilloscopes and accessories, graphical multimeters (wavemeters), programmable power supplies, spectrum analyzers, frequency counters, breadboards, milliohmmeters, infrared temperature probes, SMT products, instrument carts, soldering and desoldering systems, magnifiers and inspection equipment, power analyzers, measuring tools, hand tools and reference books. Brand name manufacturers include Tektronix, Fluke, 3M, Alphametals, Hakko, Weller, Microcare, Charleswater and Chemtronics. The catalog is free.

Contact East Info/Card 162

On line:

Free resource for electronic engineers—As part of Eg³'s virtual publishing project, The EE Virtual Trade Conference (EE VTC) is available at http://www.eg3.com/vtc.htm. The EE VTC features more than 225 technical papers on topics such as object oriented programming, virtual distribution, digital signal processing (DSP), microcontrollers and microprocessors, the set top (Internet) box, world-wide web for embedded systems, embedded java, networking and embedded networking and realtime operating systems. The free software can be downloaded after registration. It can be accessed at three different web sites: www.eg3.com. www.eetoolbox.com and www.cera2. com. More information is available at info@eg3. com. Eg^3

Info/Card 163

Web site for security products—Torfino Enterprises manufactures and distributes law-enforcement and corporate security products including near-field transmission detectors, explosive detectors, X-ray machines for package screening and hand-held and walk-through metal detectors. The company is active in R&D and can custom-design equipment to the user's specifications. The web site address is http://www.torfino.com.

Torfino Enterprises Info/Card 164

Signal conditioning and data communications web site-Dataforth designs and manufactures signal conditioning and data communications products. These include the SCT line of two-wire transmitters; isolated analog and digital input and output (I/O) modules and accessories, including industry standard 5B and 7B modules; and industrial modems and modem systems. The web site includes product data sheets for the company's limited distance modems and modem systems; application notes covering technical issues; the industrial signal conditioning design guide; product announcements; a listing of the company's sales representatives and distributors; and links to other technical sites for those working in industrial data acquisition, measurement and control. The interactive site facilitates technical questions and literature orders. The site can be visited at www.dataforth.com. **Dataforth**

Info/Card 165

Bumping service design guide for IC package designers—Flip Chip Technologies, the joint waferbumping venture between Delco Electronics and Kulicke and Soffa, has a bumping service design guide for integrated circuit (IC) package designers. The guide is available for free on diskette or by downloading it from the website at http://www. flipchip.com.

The electronic document is useful for designers incorporating flip chip technology into their designs. The guide covers wafer requirements and minimum pitch capabilities. It addresses Flip Chip design standards and includes the subjects of metallurgy, available solder alloys, IC design considerations and mask data requirements. One section deals with such development directions as fine pitch, redistributions, interconnect capability and 200 millimeter wafer capability.

Also included are directions on how to obtain quotations and information on available test die. The Bumping Service Design Guide also may be obtained by calling the company. E-mail may be addressed to info@ flipchip.com.

Flip Chip Technologies Info/Card 166

PTI product line on web site— Piezo Technology (PTI)'s web site provides information on its line of resonators, diplexers, crystal filters, GPS filters and crystal oscillators. Also featured are detailed specifications, design aids, application notes, a listing of representatives and company information. The site can be accessed at http://www.piezotech. com.

Piezo Technology Info/Card 167



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RF VERIFICATION ENGINEER

Responsible for the verification of new product processes and changes to insure highest quality and productibility with the Cellular Phones manufacturing products. Be a technical liaison between design and manufacturing functions (component, factory process). Identify, evaluate and approve short-term and long-term solutions for radio/process problems. BSEE with 3 years RF design experience preferably with cellular and/or other portable phones. General radio knowledge in audio and software a plus. Experience with Spectrum/network analyzers, signal generators, RF component fixtures, communication test sets, modulation analyzers, etc. a plus. Job Code: RVE/NM

SOFTWARE - LOGIC HARDWARE VERIFICATION ENGINEER

Responsible for verification of software for new products and changes to insure the highest quality and productivity consistent with Cellular Phones manufacturing products. BSEE with 3 years software and some logic hardware design experience with cellular and/or other portable phones. 6303 up and C, C++ knowledge strongly desirable as well as some general analog experience. Job Code: SLH/NM

Please forward resumes, referencing correct Job Code, attn: Natalie Martin, to FAX: 804-948-6543, or EMAIL: <Natalie_Martin@ena-east.ericsson.se>. Additionally, we request resumes be EMAILED to <ericsson@adaptservices.com> or FAXED to 800-611-7414 for inclusion in our company-wide database. Visit our site on the World Wide Web at: http://www.ericsson.com Equal Opportunity Employer.



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The Mechanical Engineer will have at least a BSME (MSME preferred) and at least 5+ years experience in electronic packaging design for our hand held radio equipment. Experience in designing cast aluminum housing using AutoCad (3D preferred) is necessary. Experience with other electronics packaging techniques such as plastics, magnesium castings and precision sheet metal would be a significant plus. The chosen applicant will design rugged packages for our hand-held radio equipment. US citizenship is required.

DSP ENGINEER

The ideal candidate will have a BSEE/BSCS degree and at least 5 years of experience in DSP algorithm and software development for portable radio applications including baseband (audio) filtering and processing. IMBE and/or CVSD encrypted voice processing, digital data processing and modulation/demodulation. Experience developing DSP applications for the Analog Devices ADSP21xx or Motorola 563xx processor family is a plus. The position also requires proficiency using the PC for engineering design and administrative tasks. US citizenship is required.

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