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#### DECEMBER 1975



#### this month

•	S-line frequency	8
	synthosizor	
٠	introduction to	
	microprocessors	32
•	1296-MHz bandpass	
	filters	46
•	uhf frequency scaler	50
•	cumulative index	114

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# contents

- 8 Collins S-line frequency synthesizer Robert S. Stein, W6NBI
- 28 high-frequency linear amplifier William S. Skeen, W6WR
- 32 introduction to microprocessors David G. Larsen, WB4HYJ Peter R. Rony Jonathan A. Titus
- 36 squelch circuits for transistor radios Robert C. Harris, Jr., WB4WSU
- 40 2304-MHz power doubler Norman J. Foot, WA9HUV
- 46 1296-MHz bandpass filters H. Paul Shuch, WA6UAM
- 50 uhf frequency scaler Douglas R. Schmieskors, Jr., WB9KEY
- 114 1968-1975 cumulative index
  - 4 a second look
- 142 advertisers index
  - 142 reader service 58 short circuits

60 new products

- 99 flea market 52 ham notebook
- 6 stop press
- december 1975 加 3
- .....



Beginning this month we are presenting a series of articles on microprocessors by Dave Larsen, WB4HYJ, Peter Rony and Jonathan Titus, authors of the popular series of *Bugbooks*.\* Not since the development of the transistor in 1948 has any product or technology offered such an exciting promise of things to come as the microprocessor — literally a computer on a chip.

Computers in the 1960s are credited with revolutionizing the engineering and accounting fields by replacing people power with instantaneous electronic computation and retrieval. Microcomputers in the 1970s are expected to extend these benefits into areas where existing computer technology has never before penetrated, including amateur radio. Several groups are now working on microprocessor controlled vhf-fm repeaters, future OSCAR satellites will carry an on-board microprocessor for systems maintenance and control, and VE3SAT and others are already using microprocessors for ASCII communications through OSCARs 6 and 7.

Other amateur applications such as RTTY speed control, RTTY-ASCII or RTTY-Morse conversion, and automatic Morse code copiers are a natural for microprocessors. Automatic satellite tracking systems, log keeping, transmitter tuneup and control, and antenna pointing systems are other straight forward microprocessor-based systems which will see widespread use in the future. If, for example, you're a DXer

\*Bugbook I and II, Logic and Memory Circuits Using TTL Integrated Circuits; Bugbook III, Microcomputer Interfacing Experiments using the Mark 80, an 8080 system, \$35 the set from Ham Radio Books, Greenville, New Hampshire, 03048. and hear a rare VP8 on 20 meters, you would just punch VP8 into your keyboard and your beam would automatically come around to the correct heading. If you were operating on CW you would only have to tap out VP8 in Morse code – the microprocessor would convert the Morse characters into machine language, translate that into a beam heading, and turn on your antenna rotator.

Until recently the cost of microprocessor chips put them out of reach for most amateur applications, but as more and more manufacturers have gotten into the act the prices have dropped dramatically. The popular 8-bit 8080 microprocessor which was originally developed by Intel, for example, was selling for \$300 to \$400 a little more than a year ago, dropped to about \$150 this past summer, and is now available from one source for under \$30. Although these prices are still a bit high for the amateur experimenter, industry sources predict that microprocessors will sell for \$5 or less within a couple of vears, perhaps as early as 1977.

In addition to the microprocessor series in the magazine which is designed to familiarize amateurs with this important new technology, during 1976 ham radio will be presenting a series of oneday microprocessor seminars at various hamfests across the country including SAROC in Las Vegas (January 9th), Miami (January 24th) and Dayton (April 23rd and 24th). The fee for the seminar is \$50 and includes \$35 worth of books. Since seating is limited, early registration is recommended – write to ham radio for details.

> Jim Fisk, W1DTY editor-in-chief

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# presstop

<u>ANY HOPE THAT DOCKET 20282</u> — Restructuring — would be out by the end of this year has been much too optimistic. FCC Safety and Special Services Chief, Charles Higginbotham, W3CAH, feels that sometime next spring is a much more realistic target, and even then some aspects may require reexamination as additional dockets or oral proceedings such as the ARRL has requested. A tremendous amount of work has already gone into analyzing the mountain of Comments with the task far from done, and problems associated with CB's explosion aren't helping the effort.

<u>SECRECY PROVISIONS</u> of the Communications Act of 1934, Section 605, deserve a lot more attention by Amateurs than they've been getting. A strict interpretation of Section 605 forbids the disclosure of anything heard on the air except broadcast and Amateur transmissions — and that includes mentions of frequencies or any other information regarding the overheard signals!

Since This Ban applies to CB as well as other services, it could put a severe crimp in some of the recently publicized CB clean-up efforts conducted by Amateur groups.

The Intent Of Section 605 is quite clear — how likely an Amateur is to be cited for violating it is not.

<u>REQUIREMENT FOR MULTIPLE COPIES</u> for submissions to the FCC was upheld by Commissioners after consideration of a petition for its elimination submitted by W6NJU. Additional copies are necessary to insure the submission reaches all who should see it, but in their review of the requirement reductions were found possible.

Effective October 14 the number of copies required for comments on a Notice of Proposed Rule Making was reduced from 15 to 12 (original plus 11 copies) other requirements not likely to affect Amateurs were also reduced. In their rejection of W6NJU's petition the Commissioners also noted that single copy submissions are now and have been accepted although they do not receive as wide circulation as those that meet the requirement.

<u>Ham Radio/HR Report</u> readers should not forget our long standing public service offer. Send your FCC submission directly to us and we'll make all the necessary copies and mail them to the Commission for just \$1.00 per page of original document.

<u>REPEATER FUNDING</u> may become an issue with the FCC if some flagrant abuses aren't corrected. Though use of a club's <u>dues</u> to pay for repeater maintenance is well within the Amateur rules, the solicitation of money for the <u>use</u> of a given repeater or its facilities (such as autopatch) is almost certainly a violation of Part 97.112, "No remuneration for use of station."

OSCAR ORBITAL PREDICTION BOOKLET produced by W6PAJ will replace <u>HR Report's</u> monthly prediction sheets for <u>HR Report</u> subscribers in 1976. W6PAJ's handy booklet will be sent without charge to any subscriber who asks for it — dropping the monthly sheets was done in recognition that a vast number of subscribers did not use them and HR Report sheets were a duplication of effort.

6000 MILE OSCAR QSO was completed between G3IOR and W6CC! Using meteor scatter techniques on selected orbits as the Satellite was over the horizon between them, successful two-way communications were finally exchanged between the two over a period of two weeks. Congratulations to both!

<u>CIVIL SERVICE ADMINISTERED</u> Amateur Radio exams have not been as popular in the test areas as expected. At the mid-point of the two-year program (which runs until next July) no specific conclusions have been drawn and FCC Field Operations people are watching it carefully.

BARRY ELECTRONICS WILL CONTINUE as a major Amateur Radio supplier despite Barry's tragic loss in a boating accident on Long Island Sound. Barry's wife Kitty vows she and the crew will keep the business going just as before.

LAISH/BY QSLs received by several west coasters are pretty exciting wallpaper but little else. It's now considered certain that he operated only from shipboard.





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# frequency synthesizer

Robert S. Stein, W6NBI

## for the Collins 75S receiver

Complete description of a frequency synthesizer that converts the Collins 75S-series of communications receivers to general-coverage use from 3.4 to 30 MHz During the past few years, the use and application of frequency synthesis in both receivers and transmitters has increased tremendously. A quick perusal of the ads for vhf transceivers is all the evidence needed to verify this fact, although there are also many highfrequency military and commercial (non-amateur) transmitters and receivers which employ frequency synthesizers to generate specific frequencies required within those units.

The advantages of having a generalcoverage receiver in the ham shack are manifold and were discussed in a previous article describing a synthesizer for use with the Drake R-4 series receivers<sup>1</sup>. This article will describe a frequency synthesizer to supplement or replace the high-frequency oscillator crystals in a Collins 75S-1, 75S-2 or 75S-3, resulting in a receiver which covers 3.4 through

\*1849 Middleton Avenue, Los Altos, California 94022. 30 MHz. Only minor electrical changes are required in the receiver; no holes need be drilled nor other mechanical modifications made.

Before proceeding with the description of the frequency synthesizer which makes this possible, a review of the receiver conversion process is in order. The 75S-1, 75S-2 and 75S-3 receivers all utilize identical crystal-oscillator and first-mixer circuits, so that the discussion is applicable to any one of the receivers.

The local-oscillator (LO) frequency injected into the first mixer is 3.155 MHz higher than the low-frequency end of the desired 200-kHz tuning range. Since the high-frequency oscillator is crystal controlled, this requirement is translated to a crystal which will generate the proper frequency. For example, the 3.8- to 4.0-MHz band requires a 6.955-MHz crystal (3.8 plus 3.155 MHz), which is supplied with the receiver. Collins specifies that the receiver

S-line frequency synthesizer with some of the 128 crystals from the Collins CP-1 crystal pack, which it replaces.



will tune from 3.4 to 30 MHz with the proper crystal. It should be noted that for receiver frequencies above 12 MHz, frequency doubling takes place in the plate circuit of the crystal oscillator; therefore the *crystal* frequency is one-half the frequency injected into the first mixer. Nevertheless, the *injection* frequency is always 3.155 MHz above the lower band edge.

In order to cover the entire range of 3.4 to 30 MHz in 200-kHz increments. 133 crystals would be required, starting with a 6.555-MHz crystal for the 3.4- to 3.6-MHz band, a 6.755 MHz crystal for the 3.6- to 3.8-MHz band, and so on. Even with the 28 crystal positions available in the 75S-3A, it is obvious that a complete set of crystals would not only be impractical to use, but prohibitively expensive. However, if we can generate frequencies of 6.155 through 32.955 MHz every 200 kHz, and substitute them for the crystals in the hf crystal oscillator, we can achieve all-band coverage within the specified tuning range of the receiver. The frequency synthesizer to be described does exactly that.

#### basic phase-locked loop frequency synthesizer

Although the basic phase-locked loop frequency synthesizer has been explained in previous articles, a brief review at this time will simplify the detailed explanation of this specific synthesizer. Fig. 1 shows the basic phase-locked frequency synthesizer. A stable reference frequency is applied to one input of a phase comparator. The output of the phase comparator is a dc voltage which passes through a lowpass filter and controls the frequency of a voltage-controlled oscillator (vco). The oscillator generates the desired frequency, which may be any multiple of the reference frequency. The vco output is also applied to a frequency divider whose function is to divide the vco output frequency to the same frequency as that of the reference oscillator.

Let's assume that the reference oscillator frequency is exactly 5 kHz and that an output frequency of 6555 kHz is required. If we have a divider or programmable counter which will divide by 1311, the signal input to the phase comparator will also be 5 kHz when the vco output is exactly 6555 kHz. This is accomplished by the phase comparator producing a dc output which "tunes" the vco until it is exactly 6555 kHz. The divided vco frequency is then exactly 5 kHz, the same as the reference frequency. Thereafter, the vco output will stay at 6555 kHz; any variation from this frequency changes the signal input to the phase comparator, which in turn produces a dc output change and brings the vco back to 6555 kHz. Thus, the output frequency is locked to the reference frequency, and has essentially the same stability as the reference oscillator.

By using a frequency divider which can be programmed, it is possible to obtain virtually any number of discrete frequencies which are integral multiples of the reference frequency, all of which are phase locked to the reference oscillator. The lowpass filter keeps the reference frequency from modulating the vco and establishes the lock-up time of the loop.

#### 75S synthesizer

A block diagram of the 75S hfo frequency synthesizer is shown in **fig. 2**. The loop reference is a 100-kHz crystalcontrolled oscillator, which is divided by ten and then by two, resulting in a 5-kHz reference signal which is applied to one input of the phase comparator. The other input to the comparator is the divided vco frequency, which will be discussed presently. The output from the comparator is a function of the difference between the two input frequencies and is applied to the loop filter, consisting of an active and a passive lowpass filter. The resultant dc controls the vco frequency by changing the capacitance of a varactor diode. The vco output, 6.555 to 32.955 MHz in 200-kHz steps, is amplified to a suitable level and routed to the receiver.

The vco output is also applied, via an isolating source follower, to a Schmitt trigger, which converts the amplitude and waveform of the vco output to one that is compatible with the TTL integrated circuits in the frequency divider.



fig. 1. Basic phase-locked frequency synthesizer. The frequency divider is a variablemodulus, or programmable, counter.

The vco frequency divider is a variable-modulus counter which can be programmed to divide by any factor between 1311 and 6591 in steps of 40 (i.e. 1311, 1351, 1391, 1431, etc.). An examination of the discrete vco frequencies to be synthesized will reveal that the largest common factor is 5 kHz, thereby establishing the reference frequency. Steps of 200 kHz in the vco output are obtained by changing the counter modulus in steps of 40 (40 x 5 kHz = 200 kHz). Since each vco frequency ends in 5, the least significant digit in the number by which the vco frequency must be divided to yield 5 kHz will always be 1. Therefore the first counter always provides a 1-count. The three remaining counters are programmed by the front-panel frequencycontrol switches and establish the first three digits of the frequency divisor.

Preselected binary-coded-decimal (BCD) outputs from each counter, plus the output from the Schmitt trigger, are fed to a decoder circuit, which produces Trimmer capacitor C3, in series with the crystal, permits adjustment of the crystal frequency. The output of the oscillator is shaped and buffered by a third gate, U1C.

The 100-kHz signal is divided down



fig. 2. Block diagram of the Collins 755 hfo frequency synthesizer. The only tuning controls are the front-panel TENS, UNITS, and TENTHS rotary switches.

the divided-down vco signal applied to the phase comparator. The decoder also resets the counters (actually this is its primary function), but that signal path has been omitted from **fig. 2** because it is not pertinent to overall signal flow. Details of the counter and decoder functions will be explained in greater detail under their circuit descriptions.

### reference oscillator and phase comparator

The 100-kHz reference oscillator and its frequency dividers, the phase comparator, and the loop filter are shown in fig. 3. The reference oscillator consists of gates U1A and U1B, two sections of an MC846P quad 2-input NAND gate. The gates are configured as a multivibrator and the 100-kHz signal is developed by connecting crystal Y1 as part of the signal path between the gates. to 10 kHz by U2, a 7490 decade counter. The output of the 7490 is then divided by two by one flip-flop in U3, a 7474 dual D-type flip-flop, resulting in the 5-kHz reference which is applied to pin 3 of phase comparator U4.

The phase comparator comprises U4, another 7474 dual D-type flip-flop, and the remaining gate section of U1. It compares the phase difference between the 5-kHz reference and the vco frequency divided by the counter modulus ( $f_{vco}$ /N), and produces a digital pulse output whose duty cycle is a function of the phase difference. This digital output is partially filtered by R3 and C6 to a sawtooth which is applied to the inverting input of U5.

U5 is an LM3900 quad op amp, one amplifier section of which is used as the active element in the loop filter. It attenuates the ac components of the signal from the phase comparator and thereby produces a dc output which varies in accordance with the phase difference between the inputs to the comwill be improved.) Additional attenuation of harmonics of the reference frequency is accomplished by R22, R34, C18 and C38 in the vco (fig. 4).



fig. 3. Schematic of the crystal oscillator and its frequency dividers, the phase comparator, and the loop filter, Integrated circuits are listed in table 1 (page 20). C7 must be a polycarbonate- or polyesterfilm type capacitor.

parator. The gain of the loop filter, its frequency response, and the loop lockup time are determined by the values of R3, R4, R5 and  $C7^{2,3}$ .

Additional filtering of the 5-kHz loop reference frequency is needed to prevent modulation of the vco, which would produce spurious sidebands on both sides of the desired frequency. A parallel-T filter, consisting of R6 through R8 and C9 through C11, provides a minimum of 35 dB attenuation at 5 kHz. (This figure is based on worstcase conditions using five-percent capacitors. If two- or one-percent capacitors are used, or the capacitors are selected by bridge measurement, the attenuation

#### voltage-controlled oscillator

The vco is built as a separate, shielded unit to eliminate stray pick-up from the digital circuits and from ac fields. The oscillator consists of Q1, an E300 (or equivalent) n-channel fet, in a Colpitts circuit with varactor CR25 connected in series with C38 across the tank circuit. The varactor is a Motorola MV1401 and has a ratio of maximumto-minimum capacitance of approximately ten, as compared to usual ratios of two to four for conventional varactors. (It also happens to be the most expensive single component in the entire synthesizer.) Despite the large capacitance ratio, the oscillator cannot

cover the entire range of 6.555 to 32.955 MHz without switching. This is accomplished by diode switching, using switch section S3-D of the *tens* divider switch (fig. 5).

In the zero position of the *tens* switch, diodes CR26 and CR27 do not conduct, so coils L1 and L2 are each effectively in series with a  $33 \cdot \mu$ H choke (L4 and L5) to ground. The high value of this inductance has only stray effect on the circuit; thus the oscillator frequency is essentially determined by coil L3 and the tank-circuit capacitance. When the *tens* switch is set to position 1 or 2, one of the diodes is biased into

The oscillator output is taken from the source of Q1 and coupled to the base of amplifier Q2. The amplifier, a type 2N2219 npn transistor, is a broadband stage which feeds the hf oscillator circuit in the receiver through an isolating 5-dB L-pad, R27 and R28. Also applied to the output circuit is the +12-volt power supply, which is decoupled from the vco signal by rf choke L8 in series with current-limiting resistor R32. This dc source is used to actuate a sensitive relay in the receiver, as will be explained later.

The output of Q2 is also coupled to Q3, an n-channel fet configured as a



fig. 4. Schematic of the vco. See table 1 for coil-winding data and descriptions of parts not identified on the schematic.

forward conduction and brings the low end of the associated coil close to rf ground, shunting L3 and thereby lowering the tank-circuit inductance. Resistor R21 in series with the switch arm limits diode current to a safe value. source follower. The source load is made up of two resistors, R30 and R31, which form a 6-dB L-pad in the output. The source follower drives the Schmitt trigger in the digital portion of the synthesizer and, with the L-pad, keeps



any digital signals from feeding back into the vco.

#### frequency divider

Fig. 5 shows the vco frequency divider and its associated front-panel switches. Note the use of the word divider in its singular form; the counters used in the divider circuit function as an integral circuit (no pun intended). rather than as separate divider stages such as are used to divide the 100-kHz crystal frequency down to 5 kHz. Because this is guite different from the usual frequency multiplier or divider stages familiar to most amateurs, as evidenced by the many inquiries received following publication of the R-4 synthesizer article<sup>1</sup>, it seems appropriate at this point to explain the operation of a typical variable-modulus, or programmable, counter,

Let us consider a basic two-stage frequency divider, as shown in fig. 6. Each of the counters is a decade counter, that is, a counter which produces one output pulse for every ten input clock pulses. However, each counter is presettable, which means that its count may be programmed or modified by setting its data inputs  $(D_A, D_B, D_C, and D_D)$  either high or low. The data-input subscripts indicate the binary weighting assigned to each input: A=1, B=2, C=4, and D=8. There is also a fifth data terminal,  $D_s$ ; this is the data-enable input, which must be set prior to and during the interval that the data inputs are applied. In the simplified circuit shown, we will assume that D<sub>S</sub> must be set high to enable the data inputs.

Conventional digital terminology designates the first pulse in a pulse train as 0, so that the tenth pulse, which produces an output from a decade counter, is therefore designated number 9. The total number of clock pulses,  $N_{max}$ , which can be counted before an output is produced from a ripple-through counter (another name for the circuit shown in **fig. 6**) is

$$N_{max} = N_1 \times N_2 \times \ldots N_n$$

where  $N_1$  is the modulus of the first counter,  $N_2$  is the modulus of the second counter, and so on. Since each counter in **fig. 6** has a modulus of 10,  $N_{max} = 100$ . But remember that this will be clock pulse 99, since we start with pulse 0.



fig. 6. Basic variable-modulus counter.

Now let's assume that we want the circuit of **fig. 6** to divide the clock frequency by 25. If the counters are upcounters (as are all those used in this synthesizer), their data inputs must be preset with the nines' complement of the desired divisor. (Nines' complement simply means the difference between nine and the desired count.) The preset data to be entered,  $N_D$ , is determined by the equation

$$N_D = (N_{max} - 1) - D$$

where D is the frequency divisor. Since  $N_{max}$  is 100 for our circuit,

$$N_D = (100 - 1) - 25 = 74.$$

The least significant, or units, digit corresponds to the count of the first counter, since it is counting unit clock pulses; the most significant, or tens, digit corresponds to the count of the second counter because it is counting tens of clock pulses. Therefore counter number 1 must be preset with a 4, and counter number 2 must be preset with a 7. To do this, D<sub>c</sub> (having a binary weight of 4) of counter number 1 is set high and all other data inputs are set low. On counter number 2,  $D_A$ ,  $D_B$  and  $D_C$  are set high (binary weighting: 1 + 2 + 4 = 7) and  $D_{D}$  is set low. What we have done is to preset the counters so that each is in the state which would exist following the clock pulse having the same number as the preset data. Since counter number 1 has been preset with a 4, it will produce an output after five clock pulses have occurred (corresponding to the 5 in the desired divisor of 25). Thereafter, the first counter will count by ten until D<sub>S</sub> is set high by the output of counter number 2. Similarly, because counter number 2 has been preset with a 7, it will produce an output after it has counted two pulses from the first counter, completing the count of 25. This output is applied to the  $D_{S}$  inputs of both counters and re-enables the data inputs, starting the count over.

If we analyze the operation of the counters, we can see that by presetting the first counter with a 4, the elapsed time between clock pulse 0 and clock pulse 9 was shortened by four clock-pulse intervals. In the same way, by presetting counter number 2 with a 7, the elapsed time between clock pulse 9 (the first output pulse from the first counter) and clock pulse 99 ( $N_{max}$ ) was shortened by 7 times 10 clock-pulse intervals. Assuming a clock frequency  $f_c$ , with a period  $t_c$ ,

and

$$f_{out} = \frac{1}{t_{out}} = \frac{1}{25t_c} = \frac{f_c}{25}$$

 $t_{out} = 99t_c - 4t_c - 7(10t_c) = 25t_c$ 

The preceding analysis may be extended to any number of cascaded counters and to hexadecimal as well as decade counters. However, actual opera-

tion will be limited by the propagation delays through the counters and the setup times required for the data inputs. As previously stated, the D<sub>5</sub> inputs must be enabled before and during the time period that the preset data are entered. Since the preset data are dc levels, it follows conversely that they are entered shortly after the generation of the output pulse, which is applied to the D<sub>5</sub> inputs. If the clock frequency is too high, the counters may toggle but too much time may elapse, because of propagation delays, between the output pulse following the terminal clock pulse (equivalent to pulse 99 in our basic circuit) and the arrival of the next clock pulse (pulse 0). This will prevent the data inputs from being enabled prior to the arrival of clock pulse 0, and will result in an erroneous count.

Another problem which often arises when using a circuit similar to that of fig. 6 is caused by the short duration of the output pulse. The output pulse from counters which are used in these circuits has the same width as the clock pulse. Thus the output pulse of counter number 1 is the same as the clock pulse (although with greater time intervals between pulses), and since counter number 2 is toggled by the output of counter number 1, its output pulse width will also be the same as the clock-pulse width. Furthermore, as soon as the output pulse resets the dataenable inputs, both counters resume their preset state and the output pulse disappears. This condition, along with the narrow pulse width, may not permit the data inputs to be enabled for the minimum time which is required by the counter.

The propagation delay may be minimized by decoding the BCD outputs of the counters. These outputs have the same binary weighting as the corresponding data inputs. Thus when the terminal condition of 99 is reached in fig. 7, outputs A and D of each counter will go high, causing the output of the AND gate to go high and enable the data inputs. The advantage of this circuit lies in the reduction in the delay time between clock pulse 99 and the D<sub>S</sub> enabling pulse. In fig. 6, the delay is equal to the propagation delay through the two counters, or through a total of eight flip-flops. In fig. 7, the delay is equal to the propagation delay through only one flip-flop (flip-flop A in counter number 1) plus that of the gate. This occurs because at clock pulse 98, outputs A and D of counter number 2 are high, as is the D output of counter number 1. Clock pulse 99 needs to propagate only through the first flip-flop in counter number 1 to cause output A to go high, resulting in the required enabling output from the gate.



fig. 7. Basic variable-modulus counter with decoded outputs.

This technique of decoding may be used in various circuit configurations. In many cases, it may be necessary to decode outputs which are other than those of the terminal count in order to enable the data inputs before the arrival of clock pulse 0. It may also be necessary to utilize flip-flops in addition to the decoding gate in order to enable the  $D_S$  inputs with a pulse whose width is greater than the clock-pulse width. This may result in some preset factors being unusuable, but rarely are all moduli of a variable-modulus counter utilized.

Returning now to fig. 5, we see that

the vco frequency divider is a four-stage variable-modulus counter comprising U6, a 74S196 or 82S90 presettable decade counter, and U7 through U9, each a 74196 or 8290 presettable decade counter. The signal from source follower Q3 in the vco is converted to TTL level by U11A, one section of a 7404 hex inverter. The inverter functions as a Schmitt trigger by virtue of the connection of R9 between the input and output. Additional shaping is provided by U11B, and the resultant output clocks counter U6 and both flipflops in U12.

As stated previously, only the counts of the last three counters in the chain need be varied, since U6 provides a fixed count. The counts are controlled by tenths switch S1, units switch S2, and tens switch S3. Fig. 5 shows the switches set for a receiver frequency of 4.2 MHz; the corresponding vco frequency is therefore 7.355 MHz. Since the reference frequency is 5 kHz, the vco frequency must be divided by 1471. U6 provides the least significant count of 1. The next significant count of 7 results from setting the data inputs of U7 to the nines' complement of 7, or 2. It can be seen that +5 volts are applied to pin 10 (input D<sub>B</sub>) through S1-A, while the remaining data inputs are either grounded directly or are pulled low by resistors R11 and R12, Similarly, it can be seen that U8 provides a count of 4, and U9 a count of 1 for the most significant digit.

The complexity of the switching circuits is the result of labelling the switches so that they indicate the low end of the receiver's 200-kHz tuning range, rather than the dividing count or the vco frequency. Steering diodes CR1 through CR24, in conjunction with the switches, route the 5-volt supply to the appropriate data inputs.

The BCD outputs of the counters are decoded in U10, a 7430 8-input NAND gate, the output of which is inverted by

U11C and applied to pin 3 of U12, a 74S112 dual J-K flip-flop. Both flipflops are used to re-enable the counters and require three clock pulses after pin 3 is set high by U11C. This means that instead of decoding when the BCD outputs of the counters total 9999, decoding should take place when the BCD outputs total 9996, so that the data inputs of the counters are enabled three clock pulses later, immediately following the terminal BCD state of 9999. However, I found it necessary to shorten the propagation time between the terminal clock pulse and the lastoccurring input to U10, and therefore chose to decode a count of 9995. (Note that the A and C outputs from U6 provide the least significant digit of 5.) Since this re-enables the data inputs one clock pulse early, the extra clock pulse is accounted for by presetting U6 for a count of 2, which keeps the least significant digit in the frequency divisor at 1.

Because the preset enabling pulse for the counters must be low, the  $\overline{\Omega}$  output from pin 7 of the second flip-flop in U12 is used. The complementary  $\Omega$  output from pin 9 is applied to the phase comparator for comparison with the reference frequency.

#### power supply

The synthesizer draws approximately 425 mA from its power supply, which is shown in **fig. 8** along with the interconnections of the main pc board and the vco unit.

Full-wave bridge rectifier CR29 through CR32 is supplied from T1, a 16-volt, 0.5-ampere transformer. The 12-volt supply for op amp U5 on the main board and for the vco is obtained from the output of U13, a fixed 12-volt regulator. The drop to regulated 5 volts for the logic circuitry takes place in U14, a similar 5-volt regulator. LED CR33, connected to the 5-volt supply through current-limiting resistor R35, serves as a pilot light.

#### construction

Most of the parts comprising the synthesizer are mounted on two printed-circuit boards, the main board and the vco board. The large main board contains all of the digital circuits and the phase detector, while the entire vco, except for the feedthroughs and output connector, is built on the separate vco board. Figs. 9 through 12 show the foil patterns and parts locations for the two boards<sup>\*</sup>.

The interior photograph shows the construction of the prototype unit, which is enclosed in a steel utility box measuring 10x10x3-1/2 inches (25.4x25.4x8.9 cm). It is imperative that a steel enclosure be used because of the strong magnetic field around the receiver caused by the power transformer. The phase-detector circuit and the vco in the synthesizer are extremely sensitive to ac fields, and when the unit was first enclosed in an aluminum box, it was impossible to eliminate a 60-Hz hum on received signals except when the synthesizer was placed directly in front of the receiver. Since this is hardly consistent with good "human engineering" practice, the aluminum housing was discarded and a steel box was substituted.

An enclosure was intentionally selected which was larger than might be expected, because of the sensitivity of the synthesizer to stray fields. This proved to be a wise choice (sometimes you luck out!), since the physical placement of the power transformer within the box became the next problem. Rather than fool around with compartment shielding, I mounted the transformer, rectifiers, and filter capacitor on a small piece of sheet steel. The steel shields the rest of the unit from the transformer

\*A set of two drilled and plated boards is available from the author for \$14.50, postpaid in the U.S.A. Questions will be answered if accompanied by a self-addressed, stamped envelope. field when the power supply assembly is positioned so that the steel plate is vertical and the transformer is on the side away from the main board.

Even with the arrangement described, the placement of the power supply assembly is critical. I suggest that the assembly be mounted temporarily, left-hand wall of the enclosure, with their pins extending into the interior. Apply a thin layer of silicone heattransfer compound between the regulators and the housing to aid in dissipating heat.

The three rotary switches, the power switch, and the LED pilot light are



fig. 8. Schematic of the power supply and interconnections of the assemblies comprising the synthesizer. Diodes and integrated circuits are described in table 1.

with long leads, when the unit is constructed. Then after all adjustments have been made and the synthesizer is functioning, the final location can be determined by moving the assembly around until any hum on a received signal disappears. You may find that moving it one way or the other by as little as a half-inch (1 cm) may make a big difference.

On the other hand, this problem can be eliminated, and a smaller cabinet used, if the power supply is made a separate unit and connected to the synthesizer proper by means of a cable. The choice is yours.

The two voltage regulators (U13 and U14) are mounted on the outside of the

mounted on the front panel. On the rear is the coax output connector. Four rubber bumpers are mounted on the bottom to prevent scratches from the hardware which fastens the parts to the enclosure.

When assembling the parts on the main PC board, a socket or Molex pins should be installed at U11 for the integrated circuit. It may be necessary to select a 7404, since its upper frequency limit is being pushed. But at the current price of 25 to 35 cents each, it is much more economical to buy three or four than to buy the devices which would be required for a more sophisticated Schmitt trigger. More about this later.

The main board is connected to the

frequency-control switches from 20 pads, designated A through V, along the front of the board, as shown in fig. 5. The remainder of the connections appear in fig. 8. All connecting leads to and from the board should be soldered in place on the board before connecting the other ends. Leave plenty of wire on each lead to make the connections to the parts which are not on the board so that if any troubleshooting must be done it will not be necessary to unsolder the wires. Shielded wiring is made with RG-174/U coax. All wiring, except for that between the "VCO" pad and E1 on the vco, carries dc only, making lead length noncritical. The board is mounted on four standoff posts; in order to prevent ground loops, three of the four should be non-metallic or should be insulated from the ground plane on the board, so that only a single metallic post arounds the main board to the cabinet.

The vco printed-circuit board is enclosed in a 2-1/8x2-5/8x2-3/4 inch (5.4x6.7x7 cm) mini-box. Feedthrough terminal E1 and feedthrough capacitors C17, C23, C24 and C33 are mounted on one side of the box, and J1 is placed on one end, corresponding to the leads designated in fig. 12. Use solder lugs under the outsides of the feedthrough capacitors which are to have shielded leads attached. The PC board is fastened to the side of the box on which the feedthroughs are mounted by means of small right-angle brackets which are soldered to the ground plane of the board. The feedthroughs and J1 are then connected to the appropriate pads on the board, using short lengths of bare wire.

The vco mini-box must be mounted so that there is only a single return to common ground, in order to prevent ground loops. When mounting the vco,

#### table 1. Semiconductor and miscellaneous parts list.

CR1-CR24	1N34A, 1N100, 1N270 or equivalent germanium diode
CR25	Motorola MV1401 varactor
CR26,CR27	1N658
CR28	1N914 or 1N4148
CR29-CR32	1N4001 or equivalent 50 PIV, 1 amp silicon rectifier
CR33	Hewlett-Packard 5082-4882, Motorola M∟ED655, Radio Shack 276-041 or equivalent light-emitting diode
E1	insulated feedthrough terminal
L1	5-3/4 turns no. 28, closewound on 0.211'' (5.5mm) diameter slug-tuned form (Miller 25A014-4)
∟2	10-3/4 turns no. 28, closewound on 0.211" (5.5mm) diameter slug-tuned form (Miller 25A014-3)
L3	20 turns no. 30, closewound on 0.211" (5.5mm) diameter slug- tuned form (Miller 25A014-3)
Q1	Siliconix E300, 2N5397 or 2N5398

Q2	2N2219
Q3	2N5458, 2N5459 or Motorola MPF103
51	2-pole, 5-position, non-shorting rotary switch
52	3-pole, 10-position, non- shorting rotary switch
53	4-pole, 3-position, non-shorting rotary switch
U1	Motorola MC846P quad 2-input NAND gate
U2	7490 decade counter
U3,U4	7474 dual D-type filp-flop
U5	National LM3900 quad op amp
U6	74S196 or Signetics 82S90 pre- settable decade counter
07,08,09	74196 or Signetics 8290 preset- table decade counter
U10	7430 8-input NAND gate
U11	7404 hex inverter (see text)
U12	74S112 dual J-K flip-flop
U13	7812 or National LM340-12 12-volt regulator
U14	7805, National LM340-5 or LM309K 5-volt regulator



fig. 9. Foil pattern of the main printed-circuit board.

be sure to position it so that the feedthroughs are close to the side of the main PC board on which are located the pads designated "VAR" and "VCO." The lead between E1 on the vco and the will probably have little detrimental affect). The cable between the synthesizer and the receiver *must* be the 95-ohm type or 93-ohm RG-62/U.

The power transformer should sup-



Interior of the assembled synthesizer. The power supply components are located to the left of the main PC board (top). The vco is mounted on the rear wall just above the main board (bottom right). Note the holes in the vco enclosure which provide access to the tuning slugs of the coils mounted on the vco board inside.

"VCO" pad on the main board should not be more than 3 or 4 inches (7.5 or 10 cm) long. The shields of the leads going to capacitors C17, C23 and C24 are grounded to the solder lugs under those capacitors.

The coax between J1 and the output connector on the rear of the cabinet should be 95-ohm type, such as RG-180/U or RG-195/U (although using a very short piece of 50-ohm RG-174/U ply 16 to 17 volts ac at approximately 0.5 ampere. Any higher voltage only results in greater heat dissipation in regulator U13. The method by which this voltage can be obtained by modifying an inexpensive 24-volt transformer is described in reference 1.

The numbered positions on the rotary switch knobs were made by using number transfers on the skirts of the knobs. Several heavy coats of Krylon



fig. 10. Location of parts on the main printed-circuit board.

fixative were sprayed on to keep the numbers from peeling off. The panel markings can be applied in the same manner. If you are fortunate enough to have access to a Selectric Composer, or even a good electric typewriter, the panel labeling can be typed on frisket, which is an adhesive-backed translucent acetate. The material is virtually invisible when applied to a grey panel, against which the black type effectively contrasts. Frisket is available at art-supply dealers.

#### receiver modifications

At the beginning of the article, I indicated that only minor modifications had to be made to the receiver; these are shown in **fig. 13**. The synthesized crystal frequency is introduced into the receiver via the *spare* jack on the rear apron. The added components must be placed close to the oscillator-mixer (V3) tube socket, and the shielded connection to the *spare* jack made with 93- or 95- ohm coax, e.g. RG-62/U, RG-180/U or RG-195/U.

The existing coax lead in the receiver between *bandswitch* S1 and pin 2 of V3 is disconnected from V3 and rewired to the added relay. This relay may be a reed or "crystal can" type; its coil resistance must be at least 500 ohms in order to minimize the voltage drop across R32 in the vco.

When the synthesizer is off or is disconnected from the receiver, the normally-closed relay contacts complete the circuit between S1 and V3, allowing the receiver to function as if no changes had been made. When the synthesizer is turned on, the relay is energized by the 12-volt supply in the vco through R32 and L8 (see fig. 4), disconnecting the crystals and applying the synthesized crystal signal to the control grid (pin 2) of the oscillator section of V3. The 56- $\mu$ H choke at the relay coil isolates it from the rf signal path.

A new *preselector* scale may be added to the receiver so that you don't have to consult or memorize the preselector chart in the manual. **Fig. 14** is a full-scale reproduction of the new *preselector* scale and may be cut out, or photocopied if you prefer not to mutilate the magazine.

Remove the preselector knob and

pointer and attach the scale to the front panel of the receiver, using either a spot of rubber cement or a small piece of double-sided sticky-back tape in each corner. The scale shows the approximate settings of the *preselector* control; the letter at the end of each scale segment indicates the *bandswitch* position to be used.



Construction of the vco sub-chassis. Inductors L1, L2 and L3 are at left. Output connector is at right. Feedthrough capacitors and input connector are on rear panel. All other components are mounted on the printed-circuit board at bottom.

#### alignment and test

After all wiring and connections have been checked and rechecked, the synthesizer is ready for the few adjustments necessary to set the vco on frequency. The only test equipment absolutely necessary is an electronic voltmeter, although a frequency counter and oscilloscope can be helpful.

Apply power to the synthesizer and

check the supply voltages to make sure that they are within five percent of the nominal values. Then make sure the reference oscillator is working by bringing a lead from the receiver antenna jack close to the crystal. Harmonics of the 100-kHz oscillator should be heard in the receiver. The oscillator may also be checked with a scope; 100-kHz square waves should be observed at pin 3 of U1, and 5-kHz square waves should be present at pin 9 of U3. If the oscillator is not working, adjust trimmer capacitor C3, although it is not necessary for the crystal to be oscillating at exactly 100 kHz at this time.

Connect an electronic voltmeter between ground and feedthrough capacitor C17 on the vco. Set the rotary switches to 9.8 MHz and adjust the tuning slug of L3 until a meter reading of 10 volts is obtained. Rotate the units switch toward zero, noting that the voltmeter reading drops with each change in the switch setting until position 3 is reached. Then rotate the tenths switch to zero, noting that the voltage continues to drop. (Actually, any switch setting below 3.4 MHz is invalid, since it is below the tuning range of the receiver preselector.) A frequency counter connected to the output of the synthesizer should indicate approximately 12.955 MHz with the frequency switches set to 9.8 MHz, and 6.155 MHz with the switches set to 3.0 MHz. The exact frequencies will be obtained only if the crystal is set to exactly 100 kHz, which adjustment is not made until the vco is aligned.

Next, set the rotary switches for a frequency of 19.8 MHz, and adjust the slug in L2 for a voltmeter reading of approximately 10 volts. *Do not touch the slug in L3*. Again turn the *units* switch toward zero and note that the voltage drops at each switch position, including position 0. Turn the *tenths* switch to 0 and make sure that the voltage also decreases with each step, A

counter should indicate about 13.155 MHz and 22.955 MHz respectively for the minimum and maximum *units* and *tenths* switch settings.

Finally, set the rotary switches for a frequency of 29.8 MHz and adjust L1 as described in the preceding adjustment. The frequency range of the vco with the *tens* switch in position 2 is 23.155 to 32.955 MHz. If you find that it is not



fig. 11. Foil pattern of the vco printed-circuit board.

possible to obtain a 10-volt reading on the voltmeter at switch settings of 29.8 MHz, but that at some lower frequency the loop starts to lock up (as indicated by incremental changes in the voltage as the *tenths* or *units* switch positions are changed), you must change U11. I tried four 7404 hex inverters in the circuit; two worked at the highest frequency and two quit at about the 26-MHz switch settings. Thus there is every probability of getting at least one better-than-average IC out of three or four.

Connect the synthesizer output to the *spare* jack on the receiver, using a cable made from 93- or 95-ohm coax, Turn on the receiver and synthesizer and set the synthesizer switches to one of the WWV frequencies suitable for good reception. Set the receiver bandswitch and preselector control to the settings specified for the frequency selected. WWV should be heard when ing on the synthesizer and setting its switches to the desired frequency. Then set the receiver *bandswitch* and *preselector* control to the appropriate positions and tune.

One minor difference will be noted when using the synthesizer. On the



fig. 12. Location of parts on the vco printed-circuit board.

the receiver is tuned to zero. Then allow the synthesizer and receiver to warm up for about a half-hour.

Wrap a few turns of one end of an insulated wire around V2 in the receiver and bring the other end close to the 100-kHz crystal in the synthesizer. Carefully adjust the crystal trimmer capacitor in the synthesizer to zero-beat with WWV. It may be necessary to retune the receiver slightly when doing this because changing the frequency of the crystal changes the synthesizer output frequency, which is now the receiver hfo frequency.

That completes the alignment – you now have a general-coverage receiver.

Operating the receiver with the synthesizer involves no more than turn10-meter band, the 200-kHz segments start at 28.0 MHz and progress in 200-kHz increments so that you tune from 28.4 MHz, 28.6 MHz, etc. In other words, while each segment throughout the synthesizer range will start with an even *tenths* digit, the crystals supplied with the receiver set the 10-meter segments at 28.5, 28.7, and 28.9 MHz.

There is one precaution which may be necessary. Even with the prototype unit enclosed in a steel box, there was still a very small amount of 60-Hz pickup from the receiver transformer when the synthesizer was placed next to either side of the receiver. (The condition also exists with the synthesizer on top of the receiver, but this arrangement would block the heat convection flow from the receiver and should not be used anyway.) Simply moving the synthesizer 3 to 4 inches (7.5 to 10 cm) away from either side eliminated the stray pick-up. It is entirely possible that this condition may not manifest itself with all receivers, and it will undoubtedly depend on the physical locations of the assemblies within the synthesizer cabinet. In any event, the synthesizer is still close enough to the receiver for convenient operation.

#### conclusions

The synthesizer satisfies all the requirements necessary to make any Collins 75S a general-coverage receiver. Spurious signals are down a minimum of 80 dB on all frequencies, and are down better than 90 dB on most. The major spurs appear 10 kHz either side of the incoming signal, and are caused by the second harmonic of the 5-kHz reference frequency. The reference frequency itself is weaker than the harmonic because of the attenuation provided by the parallel-T filter. Although the suppression of the spurious sidebands was achieved at the expense of fast lock-up time, a one- or two-second lock-up is of little consequence, since it takes that long to move your hand from the synthesizer switches and tune the receiver.

The synthesizer has not been used with a 75S receiver operating in transceive mode with a 32S transmitter, al-



fig. 13. Wiring changes to be made to the Collins 755 receiver. Make sure that the relay will pull in when it is connected in series with a 110-ohm resistor to a 12-volt dc supply.

#### PRESELECTOR



fig. 14. New receiver preselector scale for the Collins 755 receiver.

though there is little reason to doubt that it will work. There should be sufficient sideband attenuation to keep spurious outputs from the transmitter at least 60 dB down. The only possibility of trouble might be rf getting back into the synthesizer from the transmitter, which would be simply a shielding problem. However, until and if new amateur bands are forthcoming, there is no reason to use the synthesizer for transmitting except possibly on part of the 10-meter band.

#### acknowledgements

The following were instrumental in enabling me to complete this project; without their assistance this article would never have been written: Cliff Buttschardt, W6HDO, for the use of his 75S-3 receiver; Duke Moran, W6SPB, who etched the prototype PC boards; Paul Zander, WB6GNM, for his invaluable help in the design of the phaselocked loop; and Bob Melvin, W6VSV, who listened to my problems and even made a suggestion or two.

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ham radio



## 100-watt linear amplifier for QRP rigs To dispose of the

A compact rf amplifier for ultra low power amateur transmitters

W. S. Skeen, W6WR\*

To dispose of the first question apt to be asked - "Why add a linear amplifier to a QRP rig since it defeats the whole idea of QRP operation?" - I'd like to say that while 2 to 5 watts can do wonders during the day, night operation is a different story. The prevailing sunspot activity precludes the predictable propagation conditions of 10 or 15 years ago, even on the 40- and 80-meter bands. A little boost to the output of a QRP rig means the difference between fun and drudgery during nighttime operation. When good conditions return, a linear amplifier probably won't be needed for low-power work.

I built this amplifier to augment a homebrew rig that didn't live up to my expectations — the rig had only about 5 watts output on ssb. The linear amplifier described here should prove to be a useful adjunct to low-power transmitters in the 2 to 10 watt range.

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#### circuit

The schematic (fig. 1) is simple, effective, and uncluttered. A groundedgrid, grounded screen circuit is used without the usual blower for tube cooling. Any of the Eimac 4X or 4CX tubes will perform equally well.

In the late 1950s, I witnessed some tests at Eimac that were run to see what these tubes would do without forced air cooling. The tests indicated that the tubes would dissipate 60 to 70 watts under key down operation — however, the tubes were mounted *in the open*, with no restriction to ambient air flow. Under intermittent operation, it appears



fig. 1. QRP linear schematic. Any of the 4X or 4CX series of tubes may be used. Up to 50 watts dissipation is possible without a blower providing tube is mounted in the clear.

that a tube of this family could safely dissipate at least 50 watts; perhaps a little more if cooling fins are provided. Again, the qualifier is: unrestricted air flow around the tube. A further advantage is that the heater-cathode isolation in these tubes is excellent; no filament chokes are required at this power level.

One other precaution should be observed. Although the heater is rated at 6.0 volts  $\pm 5\%$ , it is recommended that 6.0 volts be considered the upper limit. A 50-ohm, 10-watt resistor in series with the primary of a 6.3 Vac, 2.5 amp filament transformer should do the trick. The heater contributes a large part of the heat to be dissipated, and tube life is prolonged by keeping the heater voltage on the low side.

A noninductive, 1-watt carbon resistor (R1) of a few hundred ohms is provided for situations where excitation is excessive with no provision for reducing it. The resistor should be selected to obtain recommended operating conditions. While this amplifier is a two-band affair for 80 and 40 meters, additional taps can, of course, be provided for other bands on the pi-net output coil.

#### operating conditions

The amplifier has a power gain of about ten with both grids grounded, so 5 watts input should yield about 50 watts output, with a plate current of 100 mA and  $E_b$  at 1 kV. This current is 100 mA as read on the meter in the CW mode. Although up to 150 mA can be obtained with 7 watts input on CW, it is recommended that the series grid resistor be switched in to hold the plate current to 100 mA on ssb or 150 mA on CW. As with any low duty cycle amplifier, don't hold the key down longer than necessary.

Static plate current (no drive) is about 10 mA. Linearity could be improved by a higher idling current, but observations with a spectrum analyzer indicate that, with 10 mA static plate current, the bandwidth is entirely acceptable, and reports have been universally good.

#### construction

An aluminum chassis, 2x6x9 inches (5x15x23cm) in an LMB cabinet constructed with perforated aluminum for sides top and bottom, easily contains the amplifier with power supply. The



Chassis layout. Power transformer (upper right) is a 50VA isolation transformer. Note air space around tube.

LMB cabinet (model CO-2) measures 6½ inches high by 10 inches deep by 13 inches wide (16.5x25x33cm) excluding hood. The chassis was purposely selected to improve air circulation. The tube socket is mounted as close as possible to one rear corner, both for short leads from coax connectors and again to improve cooling by air circulation over the chassis edge (see photo).

While the built-in screen bypass capacitor of the SK-600 socket is superfluous, open space around the tube pins permits air flow around the header (tube base). Old timers will remember that these tubes also fit in a loctal socket. A 4-inch (10.2cm) square piece of perforated aluminum with chassis cutout should also be suitable. The grid resistor shorting switch, if used, should be mounted close to the tube, which means a shaft extension. The rf chokes are ordinary gardenvariety 2 mH, 100 mA chokes with the exception of the plate choke; but even here, tests indicated that the smaller chokes should hold up.

The 10- $\mu$ H pi-net coil (46 turns, 7/8 inch [2.2cm] OD, 3 inches [7.6cm] long, air wound) is barely large enough to cover the low end of 80 meters and is tapped at slightly less than one-half for 40 meters. The coil is mounted on the switch. A paralleled BC tuning capacitor suffices for the output. Additional fixed capacitance to total 1000 pF can be used, if necessary, for 80 meters.

#### power supply

A 50-VA isolation transformer is used with 120 Vac input and 240 Vac output to a voltage tripler arrangement that provides the 1-kV plate supply. Inspection of recent catalogs indicates that 115/230 V primary, 115 V secondary transformers are about all that are available now (about \$10). In this case, the secondary may be used for the primary with a slight loss in output voltage and regulation. The filter capacitors and diodes mount under the chassis, and since there isn't much else there, no under chassis photograph is provided. A separate heater transformer and switch are provided. The tube heater should be allowed to warm up at least a half minute before applying plate voltage. Static plate current provides "bleeder" protection.

#### summary

This small linear compares favorably, both in size and performance, with commercially built units of the same power class. It has held its own with other 200-watt-plus units and has provided many solid contacts during the worst interference hours of the evening.

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## an introduction to microprocessors

Microprocessors are probably the single, most exciting development in the entire field of electronics, and in this article, the first of a series on microprocessors, we would like briefly to compare them to programmable calculators for typical laboratory applications.

The best description of what a microprocessor is, and isn't, was given by Laurence Altman in a recent issue of *Electronics*:<sup>1</sup> "A microprocessor is not a computer but only part of one. To make a computer out of a microprocessor requires the addition of memory for its control program, plus input and output circuits to operate peripheral equipment . . . What a microprocessor is, then, is the control and processing portion of a small computer or microcomputer. Moreover, it has come to mean the kind of processor that can be built with LSI mos or, more recently, bipolar circuitry, usually on one chip. Like all computer processors, microprocessors can handle both arithmetic and logic data in bit-parallel fashion under control of a program. But they are distinguished both from a minicomputer processor by their use of LSI with its lower power and costs, and from other LSI devices (except calculator chips) by their programmable behavior."

Thus, a microprocessor is not a totally self-contained computer-on-achip, nor is it able to complete with and replace the central processing unit (CPU) within a computer. Existing David Larsen, WB4HY3, Peter Rony and Jonathan Titus\*

microprocessor chips are simply much too slow for such applications. The niche that microprocessors will soon fill is in the creation of "smart" input/ output devices to a computer that relieve the computer of the drudgery associated with the data acquisition from and the control of such devices. In other words, microprocessors will shortly become very important tools in computer interfacing, a trend that will accelerate as the price of microprocessor chips declines, as more individuals develop the capability to handle such chips, and as more manufacturers incorporate such chips in laboratory instruments and other types of devices that communicate with computers,

The advantages of interfacing with microprocessors are at least fourfold:

1. Microprocessor communications are simple. The communications capability of a microprocessor system is a big point in its favor. Most such systems come with a built-in asynchronous serial port, and thus can communicate with teleprinters or with any device that also has an asynchronous serial port. The microprocessor is not inherently limited to only a single asynchronous port; it is

\*Mr. Larsen, Department of Chemistry, and Dr. Rony, Department of Chemical Engineering, are with the Virginia Polytechnic Institute and State University, Blacksburg, Virginia, Mr. Titus is with Tychon, Inc., Blacksburg, Virginia. very easy to add more such ports and thus permit the microprocessor system to communicate serially with other external devices such as laboratory instruments that are interfaced with Analog Devices' Serdex modules.

Microprocessor systems have parallel input ports for inputs from various digital sensor instruments, including voltmeters, panel meters, frequency meters, and counters. Any type of digital circuit that can supply parallel digital data can be used in conjunction with a microprocessor system.

2. Microprocessor systems are inexpensive. Such systems currently range in price from several hundred dollars to several thousand dollars, depending upon the capability of the system. They are available from Intel, Prolog Corporation, E & L Instruments, Control Logic, and other companies. The number of manufacturers that offer microprocessor systems is increasing rapidly.

3. Microprocessor systems are flexible and powerful. Microprocessors have the ability to make decisions. (Is an input value from a digital sensor too high or too low? If it is too high, then open a valve and release pressure on the system. If it is too low, then open another valve and add gas to the system.)

Microprocessors use software to replace hardware; i.e., microprocessor programs replace complicated hard-wired random logic digital electronic circuits that perform a variety of functions, including sequential logic, non-sequential logic, simple arithmetic calculations,

This the first of a new series of articles on the subject of microprocessors which we will be presenting in future months. Material presented here is reprinted with permission from *American Laboratory*, June, 1975, copyright © International Scientific Communications, Inc., Fairfield, Connecticut, 1975. and comparison of digital signals. Manufacturers of microprocessor systems provide you with both read/write memory, for temporary data and program storage, and with read-only memory, which is easily programmed with the aid of a PROM programmer. Once you have written and tested a program using read/write memory that can acquire data and perform desired control operations, you can "burn" it into a programmable read-only memory (PROM) IC and then use that chip day after day to operate the microprocessor system.

You never have to worry about a power failure causing your program to be erased. The program can remain in the PROM for up to twenty years; it is always available for reloading into a read/write memory. The program can be easily modified to accommodate changed data acquisition or control requirements. You can develop a whole repertoire of PROM chips to accomplish different functions.

4. Microprocessor systems are capable of handling most laboratory data acquisition requirements. Current microprocessor systems can acquire digital data at the rate of five hundred 16-bit words per second. Higher data acquisition rates are occasionally claimed by manufacturers, but they frequently overlook the real software overhead that is needed, for example, to input the data, check if the data are ready, and compare the data to make sure that they are within the right range of values.

In the area of mathematical computations, microprocessors can perform integer multiplications and divisions, i.e., 3 times 4 or 5 divided by 7, with reasonable accuracy. A floating-point package available with the 8-bit Intel microprocessor allows you to perform additions, subtractions, multiplications, and divisions over the range of  $\pm 10^{32}$  to  $\pm 10^{-32}$ . This package requires four read-only memories, which means that 1000 words of your microprocessor are dedicated to the floating-point package. Execution times are slow, so you must worry about the following types of questions: Do you acquire a data point and then operate upon it and still have sufficient time to acquire the next data point? Or must you store a complete block of data and then operate upon the block as a whole? If you store a block of data, how much additional memory is required for the microprocessor? Finally, is the system sufficiently complex and expensive that it can be replaced by a minicomputer or programmable calculator?

The strong point of the microprocessor is that it can perform control functions quickly, easily, and inexpensively. The microprocessor can turn devices on and off. It can regulate physical parameters such as temperature, pressure, velocity, and flow. Since it lacks special functions such as log,  $\chi^{y}$ , sine, cosine, square root, hyperbolic sine, and hyperbolic cosine, it cannot perform sophisticated mathematical computations. This is one reason why many individuals are looking very seriously at programmable calculators, which start in the vicinity of \$3000; are available from Wang, Tektronix, and Hewlett-Packard; and allow the user to program with complex functions such as sine, cosine, log, and  $\chi^{y}$ . The programmable calculators, however, are not nearly as convenient to use as microprocessors in the control of equipment and processes,

As a final point, we would like to caution you about making any longterm decisions concerning both microprocessors and programmable calculators. The comments above apply to today's technology, which is precisely what you can do today. The price/ performance ratio changes from day to day so that a decision that is valid today may not be the same one that would be proper in a month or a year from now; e.g., 8-bit bipolar microprocessors now available from Intel have cycle times of 50 nanoseconds. This speed is a little bit difficult to precisely define for the user, but it represents probably a decade of improvement in overall microprocessor speed when compared to any microprocessor available a year ago.

If you can postpone your problem, you may find that you can solve it differently and/or less expensively a year from now. Digital electronics is without doubt the fastest changing technological field today. You, as an amateur, engineer or scientist, will be a major beneficiary of the changes that are occurring. However, to take proper advantage of the new technology, you will have to spend some time learning the jargon and understanding the tradeoffs that can be made.

Microprocessor equipment, if cared for properly, has an operational life of at least ten years but a functional life that may only be several years. A reasonable strategy would be to postpone the purchase of a microprocessor until the price/performance ratio justifies a purchase, and then to go ahead and purchase a system with the knowledge that the same system will probably cost at least 20% less for the same performance a year later. We believe that not too much time will pass before all of us who are involved in research or manufacturing and depend upon instrumentation will have to take advantage of the power of microprocessors if we are to continue to have viable products or research programs.

We recommend that you give careful consideration to the ability to interface newly acquired digital instruments to future ones that will come on the market within the next several years. We emphasize again that the existence of asynchronous serial ports on your digital instruments will allow you to hedge your bets for the future.

#### reference

1. L. Altman, "Single-chip microprocessors open up a new world of applications," *Electronics*, April 18, 1974, page 81.

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## squelch circuits

Robert Harris, Jr., WB4WSU, 801 Tucson Road, Virginia Beach, Virginia 23462

During no-signal conditions, the audio output of a receiver is random and unpleasant noise. When a signal is received, the gain of the receiver is reduced or limited by agc action, and the level of noise output is reduced. The greater the signal strength, the lower the noise output, and hence the term "receiver quieting," By adding circuitry which detects the degree to which the receiver has been quieted, and by using this circuitry to mute or un-mute the audio output, squelch may be added to the receiver.

Note, that with the squelch I have just described the operator may adjust the sensitivity of his receiver in terms of a minimum signal-to-noise ratio needed to produce an audio output signal. By making this signal-to-noise ratio sufficiently high, the operator can be sure that whenever the receiver produces an audio output it will contain a signal of a



fig. 1. A typical ratio detector found in many transistor radios. Age voltage may be taker from the (+) or (-) terminals.

## for transistor radios

Agc-activated squelch

can easily

be added

to portable

transistor radios

Inexpensive transistorized portable radios can become excellent monitor receivers for vhf operators (a-m and fm) with the addition of one of the simple squelch circuits presented in this article. The squelch will get rid of the constant and fatiguing hash and noise usually put out under no-signal conditions, making the portable a much more useful and enjoyable radio to listen to. I have had much success in adding the circuits shown here to several portables. It should be possible to adapt this same basic approach to just about any existing portable receiver.

A brief explanation of squelch circuitry seems appropriate at this point.



fig. 2. The audio section of most portables will closely resemble the circuit shown here. Point A in Q2's emitter is a control point for muting the audio output.

certain minimum readability. At first this might sound like intentionally reducing the sensitivity of your receiver, but this is not so. With sophisticated circuits, the opening of the receiver squelch alerts the operator to the presence of marginal level signals that might otherwise have gone unnoticed in the noise. Unfortunately, these noise-

operated squelch circuits are somewhat complex, and they are beyond the scope of this article.

Another method of producing squelch action is to make use of the agc or other signal level dependent voltages to control audio muting. The only drawback with this approach is that sufficiently strong noise or interference will also open the squelch. However, for the purpose intended here they work guite acceptably.

#### detector

Most inexpensive portable receivers use the common ratio detector similar to the one shown in fig. 1. This detector develops significant positive and negative voltages during signal conditions, either of which may be used for control of the audio muting. Generally, the audio section of a portable receiver will closely resemble the circuit of fig. 2. Audio from the detector is coupled to  $\Omega$ 1, a preamplifier, (which is sometimes omitted in inexpensive sets). The output is coupled through the volume control



to the driver stage, Q2, which in turn drives the output stage. These sections are easily located by finding the audio transformers associated with them, and it is seldom necessary to resort to a schematic to find the desired stages. plete muting are shown in fig. 4. In these circuits, the emitter signal path of the driving transistor is not broken, but the biasing of the driver is upset when no signal is present. But with even a small signal present, the bias is sharply



#### simple squelch

The point marked X in the emitter of Q2 is a convenient point to add squelch control to the audio stages. By breaking the circuit at this point and adding the muting circuit of **fig. 3A**, a simple squelch circuit is obtained. In some cases, small amounts of signal or noise will leak through even when this stage is supposedly squelched. Also, an increase in distortion may be noticed at high volume levels. A variation of this circuit is also shown, using an npn transistor, in **fig. 3B**.

#### improved design

Somewhat more positive acting squelch circuits which do not tend to cause distortion or suffer from incom-

returned to normal and audio output is restored.

#### conclusion

The several approaches to agccontrolled squelch shown here can be easily adapted to most portable radios. Receivers using both npn and pnp transistors may be accommodated, and junk box transistors seem to work a great percentage of the time. If you are unable to locate a source of agc voltage, do a little poking around with a vtvm until you find a voltage source that varies with signal strength. That is all that is needed to add squelch to a portable radio, making it a much more useful and enjoyable low cost monitor receiver.

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## 1152to 2304-MHz power doubler

Vorman J. Foot, WA9HUV

Construction of a single-tube frequency doubler for 2304 MHz that provides 5 dB power gain A 2C39 power amplifier capable of providing 30 watts output on 2304 MHz was described in the February, 1975, issue of ham radio.<sup>1</sup> Its design involves a combination of the best characteristics of various experimental 2.3 GHz amplifier models I have built and tested over the past three years. Each succeeding version differed from the previous one in ways which both improved performance and simplified construction.

During the same three-year period, on-the-air tests over a ten-mile path were performed between WA9HUV and both W9DCN and K9CNN, first working 432/2304 crossband, and later using 2304 MHz two-way. Signals were well over S9 on 2304 MHz, in spite of the 1296-MHz antenna used by W9DCN. Contacts over longer distances have

\*293 East Madison Ave., Elmhurst, Ill. 60126.

40 december 1975



fig. 1. Circuit diagram for the 1152 to 2304 MHz power doubler using a 2C39 which provides approximately 5 dB gain. Rf chokes are 8 turns no. 18 tinned copper, airwound on 3/16" (5mm) mandrel, turns spaced slightly.

been solicited, but none have yet been tried. It is hoped that this article, together with the preceeding one which described the 30-watt power amplifier, will provide the impetus necessary to develop new interest in the 2304 MHz band.

#### frequency doubler

Having arrived at a reasonably good basic design, attention was focused on

Complete cathode partition assembly showing the heater/cathode line (left), piston tuner (center) and cathode coupler (right).



developing a companion doubler stage capable of driving the power amplifier to full power output with drive to spare. Rather than starting from scratch, it was decided to convert one of the earlier power amplifiers into a doubler by lengthening the cathode cavity to 1-3/8 inch (35mm). No changes were made to the amplifier plate circuit. The resulting doubler circuit is very similar to the power amplifier.

Because the doubler plate circuit is identical to that of the companion power amplifier, only the doubler cath-



fig. 2. Heater/cathode assembly uses parts from surplus 2C39 amplifier. Use the mounting plate as a template to locate the four 2-56 tapped holes for assembly with the cathode partition.

ode circuit will be described here. Details of the plate circuit can be obtained from reference 1.

#### heater-cathode assembly

The heater-cathode assembly shown in **fig. 2** is nearly identical to the one used in the amplifier except that the heater-cathode line extends into the cavity 1-1/16 inches (27mm). The 2-56 brass flat-head machine screw holds a solder lug to connect the cathode side of the heater to the appropriate circuitry (this detail was omitted from the amplifier article). Attach the screw to the plate with a 3/16 inch (4.5mm) hexagonal nut and then sand the inside surface of the plate flat to make sure the screw head does not project beyond the surface of the plate. Finally, position the plate over the finger-stock assembly and solder the two together as shown in **fig. 2**.

The completed heater-cathode assembly should be insulated from the cathode partition with insulating shoulder washers and 0.005 inch (0.1mm) Teflon sheet.

#### cathode piston tuner

The cathode partition is identical to the one described for use with the amplifier and is shown in fig. 3. Rather than using a brass bushing from an old volume control for the piston trimmer, a 3/4 inch (19mm) diameter brass cylinder 5/8 inch (16mm) long is soldered to a length of 1/4 inch (6.5mm) diameter brass rod. Then a 1-1/4 inch (32mm) length of 3/8-32 threaded brass sleeving is slipped over the 1/4 inch (6.5mm) shaft and soldered in place as shown in fig. 4. Soldering should be done with the aid of a propane torch, using solder sparingly. Finally, the tuner and sleeve

#### Exterior view of the cathode partition.





fig. 3. Cathode partition. Holes marked with the letter C are screwdriver clearance holes to facilitate assembly. Material is 0.093'' (2.5mm) brass.

assembly are screwed into the tuner bushing from inside the cathode partition.

If 3/8-32 threaded brass tubing is not available, use 3/8-28 threaded lamp fixture brass tubing which is obtainable in most hardware stores. In this case, the tuning shaft should be made of 5/16 inch (8mm) diameter brass rod to fit inside the lamp hardware. Test the threaded tubing with a magnet to make sure it is not brass-plated steel. Before reassembly with the cathode cavity, the cathode input coupling circuit is assembled as described in the next section.

Helical springs are used to put pressure on the threads of the tuning piston trimmer threads. These springs, which are used on the amplifier as well as the power doubler, are 9/32 inch (7mm) inside diameter. A brass collar with set screws is used at the far end of the tuning shaft to place the spring in compression. These springs are quite important as tuning is likely to be erratic if they are omitted.

#### cathode coupling assembly

The 1/8 inch (3mm) and 5/32 inch (4mm) OD brass tubing needed to fabricate the cathode coupler (fig. 5) can be obtained from most hobby shops. The connector end of the assembly is soldered to the center conductor of the type-N coaxial connector. The 1/8 inch (3mm) end is slotted with a fine (32 teeth per inch) hacksaw blade. Spread the slotted end slightly to provide a tight slide fit with the cavity end of the coupler assembly.

The cavity end is screwed into the 3/16 inch (5mm) diameter hole in the grid cavity plate. Solder a flat brass washer on the cavity end as shown to provide a good rf contact on the inside of the cavity.

When assembling the cathode partition on the cathode cavity, slide the connector end of the coupler into the cavity end. If the instructions have been carefully followed, the two parts should slide together without interference.

#### tuning up

The circuit diagram of the frequency doubler shown in **fig. 1** is identical to the amplifier wiring diagram except for



fig. 4. Cathode piston tuner assembly. Brass rod is soldered to 3/8-32 threaded sleeve.



View of cathode cavity before installation of the cathode partition. Since an earlier model of the 2304 MHz power amplifier was modified for use as a doubler, parts in this do not correspond exactly with figs. 2 through 5.



CONNECTOR END OF ASSEMBLY





fig. 5. Cathode coupling assembly. Brass tubing can be obtained from most hobby shops.



Front view of completely assembled 1152 to 2304 MHz power doubler.

component values and the meter ranges. A 7.6-volt zener diode is used instead of the 6.3-volt unit to reduce the conduction angle of the plate current for better doubler efficiency. The quiescent (no-



"Just replace capacitor C10 . . . than you'll be back on the air."

drive) plate current should be set to approximately 25 mA by adjusting the position of the slider on the 100 ohm variable resistor.

Measurements were made using a calorimeter which indicate that the doubler has a power gain of approximately 5 dB. It is interesting to note that this doubler provides about 8 dB more power output on 2304 MHz than would be expected from a varactor doubler with the same drive power. Therefore, with less than one watt of drive at 1152 MHz, more than sufficient output is obtained to drive the power amplifier stage to full output. It is recommended that the primary winding of the doubler plate supply transformer be controlled with a variable transformer so that drive to the power amplifier can be adjusted to the desired level.

#### reference

 Norman J. Foot, WA9HUV, "Power Amplifier for 2304 MHz," ham radio, February, 1975, page 8.

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## microstripline bandpass filters for 1296 MHz Two- and three

Miniature bandpass filters for the amateur 1296-MHz band

Uhf experimenters frequently need to filter out spurious or image responses, usually with coaxial or trough-line resonators.<sup>1-5</sup> Although properly designed coaxial and trough-line filters offer exceptional skirt selectivity and minimum insertion loss, they are large and bulky and require access to sheetmetal cutting and forming equipment. The 1296-MHz filters presented here are based on printed-circuit microstripline techniques and are easily duplicated in the home workshop. H. Paul Shuch, WA6UAM, 14908 Sandy Lane, San Jose, California 95124 ■

Two- and three-pole bandpass filters for 1296 MHz are shown schematically in fig. 1. In each of the filters parallelresonant sections, consisting of microstripline inductors and piston trimmer capacitors, are loosely top coupled. The input and output striplines are tapped down on the inductors to provide a match to 50 ohms. The two-pole bandpass filter is functionally equivalent to the filters used at the input of the RF and LO ports of my 1296-MHz doublebalanced mixer.<sup>6</sup> In the design presented here, however, the coupling capacitor, C, formerly a 0.5 pF chip capacitor, has been replaced by the stray coupling capacitance between the stator ends of trimmers C1 and C2.

As can be seen from the swept frequency response curve in fig. 2, these microstripline filters are relatively low-Q devices. The steepness of the rejection skirts may be sacrificed somewhat to minimize passband insertion loss, which for this design averages around 1 dB.

#### construction

Full-size artwork for the printed-



fig. 1. Two- and three-pole microstripline bandpass filters which tune the range from 1100 to 1500 MHz. Full-size printed-circuit layouts for these filters are shown in fig. 3.

circuit microstripline filters is shown in fig. 3 and is designed for 1/16 inch (1.5mm) thick G-10 epoxy-glass printed-circuit board, double clad with 1 ounce copper.\* The unetched side of the board serves as a groundplane. Board dimensions are such that the filters mount easily in a miniature diecast aluminum box such as a Pomona 2417. The cutaway view of fig. 4 shows the method of mounting the piston trimmer capacitors on the circuit board.

With the circuit values shown, these filters can be adjusted to resonate anywhere in the range between 1100 and 1500 MHz. The easiest method to adjust for resonance at 1296 MHz is to connect a weak-signal source through the filter into a receiver, and adjust the trimmer capacitors for maximum received signal. Since the output impedance of the signal source and the input impedance to the receiver may deviate

\*Tuned and tested two- and three-pole bandpass filters for 1296 MHz are available from Microcomm. For complete specifications and prices, send a self-addressed, stamped envelope to Microcomm, 14908 Sandy Lane, San Jose, California 95124. substantially from 50 ohms, it's a good idea to temporarily install fixed attenuators at the input and output of the filter while tuning as shown in **fig. 5**. There is a certain amount of interaction between the trimmer capacitors so the adjust-



fig. 2. Swept frequency response of the twoand three-pole microstripline filters (measured with a Hewlett-Packard network analyzer and X-Y plotter). The 3 dB bandwidth is 150 MHz and passband insertion loss is about 1 dB. The 20-dB bandwidth is 320 MHz for the 3-pole filter, 570 MHz for the two-pole design.

ments should be repeated several times to insure that you have the filters tuned for minimum insertion loss.

If the filter is to be used to reduce the spurious output of a local-oscillator chain, alignment to the desired passband frequency is most easily accomplished by placing the filter in the line between the LO and the mixer and adjusting the filter for maximum indicated mixer current (fig. 6).





fig. 3. Full-size artwork for the two- and three-pole bandpass filters for 1296 MHz which are designed for 1/16" (1.5mm) double-clad G-10 epoxy-glass circuit board.

#### applications

Most amateurs who are active on 1296 MHz will probably want to have several of these bandpass filters available on their workbench. In general, accurate measurements on any two-port device are enhanced by the application of filtering at each port. Microstripline amplifiers, for example, tend to be extremely broadband; since transistors tend to have higher gain at lower frequencies, any low-frequency spurious which is applied to the amplifier will be ampli-



fig. 4. Method of mounting the piston trimmer capacitors on the microstriplines.

fied more than the desired in-band signals. It is not unlikely, in fact, for lower frequency, out-of-band signals to actually force an amplifier into gain compression. Bandpass filters at the input and output of an amplifier under test will thus aid considerably in making accurate gain and dynamic range measurements.

In operational equipment it's a good idea to place bandpass filters between each wideband stage as shown in fig. 7. The filter's 1 dB or so of insertion loss is more than offset by the elimination of image signals and spurious responses. For maximum image rejection it is recommended that the more selective three-pole filter be installed between all active stages. In the local-oscillator chain, where harmonically related spurious signals are separated from the passband by an octave or more, the simpler two-pole resonators are usually sufficient.

#### acknowledgements

I would like to thank Marvin Wahl, W6FUV, for critiquing the design of these filters, and Stu Rumley, WB6LOU, for assisting in the swept-frequency response measurements.



fig. 5. Using a weak-signal source to align a filter to 1296 MHz. The 3 dB attenuators swamp out any impedance mismatches.



fig. 6. Bandpass filter can be adjusted to the local-oscillator output frequency by tuning the filter for maximum mixer current.

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fig. 7. Installation of bandpass filters in a typical 1296-MHz transmitter and receiver. Threepole filters are recommended between active stages, as discussed in the text.

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Look what happens to the RF Power Output on our NCX-3. It was tuned for normal SSB operation and then left untouched for these "before" and "after" oscillograms.



Fig. 1 SSB signal **before** processing. See the high peaks and the low valleys. Our NCX-3 is putting out only 25 watts average power.

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Fig. 2 SSB signal after processing with LSP-520BX. The once weak valleys are now strong peaks. Our NCX-3 now puts out 100 watts of average power.

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## uhf frequency scaler

Doug Schmieskors, WB9KEY, 22065 McClellan Road, Cupertino, California

New Fairchild 11C90 decade counter IC is a direct plug-in replacement for the popular 95H90 that extends operation to above 500 MHz

Fairchild Semiconductor has introduced another outstanding IC in the 11C00 series<sup>1</sup> which should be of immediate interest to amateurs — the 11C90, a pinfor-pin replacement for the popular 95H90 that has a *minimum* guaranteed toggle frequency of 520 MHz from 0°C to  $+75^{\circ}$ C. At its best, the new 11C90 is a complete front end for a 700 MHz frequency counter (typical toggle frequency at  $25^{\circ}$ C).\*

The 11C90 uhf divide-by-10/11 prescaler makes use of Fairchild's Isoplanar II technology for high speed with reasonable power dissipation. Pins which were unused on the 95H90 decade prescaler are used on the 11C90 to provide a reference voltage which centers the input clock voltage about the switching threshold and allows direct capacitive coupling to the signal source or test antenna. An on-chip ECL-to-TTL level converter is capable of driving ten TTL loads and eliminates the need for any external output interface circuitry.

#### circuit operation

To take full advantage of the 11C90's uhf counting ability, a circuit such as that shown in fig. 1 should be built or derived from an existing 95H90 layout.<sup>2,3</sup> Pin 13 (TTL  $V_{EE}$ ) should be tied to ground (low) if the TTL output (pin 11) is used. If only the ECL output

<sup>\*</sup>The 11C90 is available now from franchised Fairchild distributors worldwide for \$16.00 in small quantities.



fig. 1. Divide-by-10 uhf prescaler has a minimum guaranteed toggle frequency of 520 MHz. Typical toggle frequency at  $25^{\circ}$ C is 700 MHz.

(pin 8) is used, pin 13 may be left open to reduce power consumption.

A reference voltage is generated internally across a 400-ohm resistor to the  $V_{BB}$  supply and is present at pin 15 ( $V_{ref}$ ). This completely eliminates any need for an external biasing network.

Pins 6 and 7 of the 11C90 are uncommitted 2000-ohm resistors which are internally connected to the mode control inputs,  $\overline{M1}$  and  $\overline{M2}$ . When tied high (+5 volts) these resistors allow the associated mode control input to be driven from TTL; if these inputs are left open or tied low, the mode control inputs offer, respectively, unterminated or terminated ECL loads to the drivers.

The mode control inputs are useful primarily when the 11C90 is employed in the divide by 10/11 mode to produce



fig. 2. Logic symbol for the Fairchild 11C90. Mode control inputs  $\overline{M1}$  and  $\overline{M2}$ , and RM1 and RM2 inputs are discussed in text. The IC includes a built-in ECL-to-TTL converter. non-standard divide ratios such as those used in pulse swallowing for frequency synthesis. The 11C90 logic symbol (fig. 2) and truth table in table 1 should aid in understanding-the device.

Circuit layout, although not critical, can be used to enhance the highfrequency operation of the 11C90. Proper power supply decoupling, broad ground connections, short signal runs, and short leads (sockets are *not* recommended) will all help the user to reap the maximum performance that has been built into the device. The 11C90 typically requires only 65 mA as compared to 90 mA for the 95H90, so it runs much cooler than its predecessor.

table 1. Mode selection for the 11C90. Low is indicated by L, high by H.

M1	M2	module divide by
L	L	11
н	L	10
L	н	10
н	н	10

#### summary

The 11C00 family of sub-nanosecond logic now consists of nine devices ranging from the 11C05 prescaler to the 11C01 gate package, and includes the 11C58, a 150-MHz voltage-controlled monostable oscillator which features a 4:1 frequency range with 2-volt dynamic range. These new devices obviously open up a whole new range of frequency synthesizer possibilities, but that's another story.

#### references

1. Douglas Schmieskors, WB9KEY, "1200-MHz Frequency Scalers," ham radio, February, 1975, page 38.

2. F. Everett Emerson, W6PBC, "300 MHz Divide-by-Ten Frequency Scaler," *ham radio*, September, 1972, page 41 (correction, December, 1972, page 90).

3. F. Everett Emerson, W6PBC, "Circuit Improvements for the Advanced Frequency Scaler," *ham radio*, October, 1973, page 30. ham radio



#### quadrifilar toroid

The prevalence of roller inductors in transmitters and antenna couplers attests to the need for adjustability. The quadrifilar toroid limits the adjustability to discrete steps but offers the advantages of small size, internal field requiring little if any shielding, and balun applications.

The ends of the four, parallel, tightly-coupled windings are connected into the desired configuration by an octal socket and tube base. Of several octal sockets I tested those with "wraparound" pins consistently measured



fig. 1. Five methods of interconnecting the four quadrifilar windings, and the measured inductance values of each configuration. Winding consists of 16 quadrifilar turns of no. 12 (2.1mm) on an Amidon T-200-6 toroid core.



Construction of the quadrifilar toroid which is based on an Amidon T-200-6 powered-iron toroidal core.

0.003 dc ohm per contact while the "edge-bite" pins varied from 0.003 ohm for a few pins to many times that value for most. Obviously only the "wraparound" octal socket is recommended and preferably in ceramic or mica-filled bakelite. If a *low-resistance* 12-point switch or plug-socket can be found, a hexifilar toroid with inductance ratios of 1, 4, 9, 16, 25 and 36 can be built.

This example of a quadrifilar toroid consists of an Amidon T-200-6 toroidal core with four windings of 16 turns each of number 12 (2.1mm) enamelled



fig. 2. Quadrifilar windings may also be used to build baluns with 1:1, 2.25:1 and 1:4 transformation ratios. wire. **Fig. 1** shows the socket connections and the measured inductance values.

In balun service the four independent windings lend themselves to several configurations; three of the simpler forms are shown in **fig. 2**. The easy access to the terminals suggests other arrangements.

The frequency response of the 1:1 balun is flat to at least 20 MHz (the limit of my sweep generator) and probably well beyond. Even at one-half and twice termination the smooth roll-off dropped only 30 and 20 per cent, respectively, at 20 MHz.

R.S. Naslund, W9LL

#### technique speeds antenna tuner adjustment

This article deals with a simple and accurate procedure for tuning or adjusting antenna tuners without using a transmitter or a standing-wave bridge. To avoid some possible confusion the term antenna tuner refers to such devices as Johnson Matchbox, Millen Transmatch, Murch Ultimate Transmatch and most similar homebuilt antenna tuners. Every ham shack should have at least one.<sup>1</sup>

In almost every technical article on antenna tuners that is published, you are instructed to make a written record of the dial settings and coil tap points for future use. If you've gone through this you know it's time consuming to search for coil tap points and tune two or three variable capacitors for each tap, trying to find the correct settings for

3. Bill Wildenhein, W8YFB, "A Low Cost RX Impedance Bridge," *ham radio*, May, 1973, page 6. each operating frequency. Furthermore, going through this procedure on the air generates a lot of unnecessary interference. I deliberately put up a four-band parallel dipole so I could avoid using (or adjusting) an antenna tuner, but because of the high swr the antenna tuner is now back in the line.

The simple technique discussed here for adjusting your antenna tuner does require an additional piece of test equipment which you may not have. However, the necessary test gear, a simple impedance bridge, can be easily built from junkbox parts. Although several RX impedance bridges have been described in the amateur literature,<sup>2,3,4</sup> the more simple antennascope<sup>5</sup> or antenna impedance meter<sup>6</sup> are suitable for

<sup>1.</sup> Ed Noll, W3FQJ, "Antenna Tuners," ham radio, December, 1972, page 58.

<sup>2.</sup> Henry S. Keen, W2CTK, "A Simple RX Bridge for Antenna Measurements," *ham radio*, September, 1970, page 34.

<sup>4.</sup> Jerry Hall, K1PLP and John Kaufmann, WA1CQW, "The Macromatcher," *QST*, January, 1972, page 14.

<sup>5.</sup> William Orr, W6SAI, *Beam Antenna Handbook*, Radio Publications, Wilton, Connecticut, page 178.

<sup>6.</sup> Robert G. Middleton, 101 Ways to Use Your Ham Test Equipment, Howard Sams & Company, Indianapolis, page 80.



fig. 3. Simple test setup speeds initial adjustment of antenna tuning unit with minimum on-the-air interference.

this application. You will also need a grid-dip meter or low power transmitter as a source of rf for the impedance bridge. A grid-dip meter is highly recommended as it will cause less unnecessary interference. impedance bridge. When finding the tap point it is suggested that the clip be held by its insulation and moved slowly up and down the coil until you see a downward movement of the bridge meter. That's the tap point you're looking for. This procedure is simplified somewhat if your antenna tuner uses a roller inductor, but the end result in either case is the same.

When the correct tap point has been found, fasten the clip on the inductor and tune the variable capacitor for as perfect null as possible on the bridge meter. Record the dial settings for future use. When a transmitter, tuned to the same frequency, is connected in place of the impedance bridge, only very minor touchup of the antenna

bridge type	frequency (MHz)	input capacitor	inductor tap	output capacitor
RX Bridge <sup>3</sup>	3.95	98	59	40
	7.25	90	68	0
	14.05	55	3	40
	21.05	90	2	10
Macromatcher <sup>4</sup>	3.95	95	60	15
	7.25	100	68	0
	14.05	35	4	24
	21.05	90	2	15
Antennascope <sup>5</sup>	3.95	90	52	10
	7.25	98	68	0
	14.05	30	4	20
	21.05	95	2	15

table 1. Comparison of Transmatch dial settings obtained with three different impedance bridges using the test setup of fig. 3.

Set up the test equipment as shown in fig. 3. If you use a grid-dip meter you won't get a reading on the swr meter, but at this point that's not important. Set the impedance bridge to 50 ohms (or 75 ohms if that's the impedance of your transmission line), tune the griddipper to the desired operating frequency and couple it to the impedance bridge. The meter on the bridge should swing upscale.

Now locate the tap on the antenna tuner inductor that causes a null on the

tuner should be required for an indicated vswr of 1:1. The data of table 1 show the results I obtained while using this procedure to adjust a Transmatch.<sup>7</sup> Note the close correlation between dial settings obtained with three different types of impedance bridges. The operating swr for all cases was very nearly 1:1. Howard Stark. WA4MTH

7. Lewis G. McCoy, W11CP, "The Ultimate Transmatch," *QST*, July, 1970, page 24.

Contraction of		CRYS DISCI	TAL FIL and RIMINA	TERS	by
$\mathbf{\nabla}$	9.0	MHz M	ODELS		K.V.G.
9.0 MHz FILTERS XF9-A 2.5 kHz XF9-B 2.4 kHz XF9-C 3.75 kHz XF9-D 5.0 kHz XF9-E 12.0 kHz XF9-M 0.5 kHz XF9-NB 0.5 kHz	SSB         TX         \$3           SSB         RX         \$4           AM         \$4           NBFM         \$4           CW         \$3           CW         \$3	31.95 45.45 48.95 48.95 48.95 34.25 53.95	9.0 MHz DIS XD9-01 XD9-02 XD9-03 9.0 MHz CR <sup>Y</sup> XF900 XF901 XF902	CRIMINATORS ± 5 kHz RTTY ± 10 kHz NBFM ± 12 kHz NBFM YSTALS (Hc25/u) 9000.0 kHz Carrie 8998.5 kHz USB 9001.5 kHz LSB	\$24.10 \$24.10 \$24.10 \$24.10 \$3.80 \$3.80 \$3.80
F-05 Hc25/u Soc	ket	.50	XF903	8999.0 kHz BFO	\$3.80
	10.7	MHz N	NODELS		
10.7 MHz FILTERS XF107-A 14 kHz XF107-B 16 kHz XF107-C 32 kHz XF107-D 38 kHz XM107-S04 14 kHz XF102 14 kHz	NBFM \$ NBFM \$ WBFM \$ WBFM \$ 4 POLE \$ 2 POLE \$	40.60 40.60 40.60 40.60 18.95 7.95	10.7 MHz DIS XD107-01 XD107-02 SOCKET (for ) Export Inquirie	CRIMINATORS = 30 kHz NBFM = 50 kHz WBFM (M107-S04) type [ s Invited	\$24.10 \$24.10 <b>DG1</b> \$1.50
VI	IF CO	NVER	TERS	UHF	
RF Freq. (MHz) + IF Freq. + N.F. (typical) Nom. Gain Power 12V D. C. $1\frac{1}{4}$ " x $2\frac{1}{2}$ " x $4\frac{1}{2}$ " + co Low loss pre-selector filte	MMc 50 50-54 28-32 2.5dB 30dB \$53.70 mnectors ers available for	MMc 144 144-148 28-32 2.8dB 30dB \$53.70 +Ot VH 432 MHz ar	MMc 220 220-224 28-32 3.4dB 26dB \$64.45 ther ranges, am F Pre Amps. W nd 1296 MHz b	MMc 432 432-436 28-32 3.8dB 28dB \$64.45 rite for details. ands.	MMc 1296 1296-1300 28-32 8.5dB 20dB \$85.95 al, to order.
	Δ	NTEN	NAS		
144/148 MHz		420-450	MHz	▲ 1250-1340	MHz
DB/2M - VERT. FOR LONGE RANG REPEATER ACCES GAIN 12.6dB REF DIP FEED 509 COAXIA	E GAIN S BA POLE FE	70/MBM/ VARIATION ND TYP ± EED 500 CC \$51.75	48 I ACROSS 0.5dB DAXIAL	1296-LY 1296 MHz LO( GAIN +20 FEED 500 CC \$51.75	DP.YAGI dBi JAXIAL
\$48.70	-	<b>\$</b> 51.75	用とうとうとうと		*****
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Transverters contain bo receiving converter all transceiver to be used band. Low Band Range High Band Range Modes Power	oth a transmitt lowing a lowe on a higher fr 146-1 442-4 FM a 12V	ing and r band equency 50 MHz 50 MHz and CW D. C.	a Vel and a	ry Happy Christ Successful New	mas Year SPECTRUM
Price Write for detailed specif F.O.B. Concord, Mass. Shipping: Via U.P.S.	\$1 ications.	79.95	S	BOX 1084 MASSACH	NTERNATIONAL CONCORD IUSETTS 01742 U. S. A.

#### burglar-proof alarm

When you are setting up a burglarproof alarm for your car, you should have an unusual alarm. The more unusual the alarm, the harder it is for a burglar to get into the car. The most important parts of the alarm are the switches used to activate it. These switches must be placed so that they are hard to find, but still allow complete protection. This means that switches should be used to prevent the car from being towed away, as well as being broken into.

After the switches have been placed, you must connect them to some sort of alarm. The alarm device must make a very noticeable sound. This requirement rules out the car's horn because people hear them constantly in a populated area. The best device for the alarm is a siren. There are two types of sirens that can be used, mechanical or electronic. Both types are suitable for the system shown in fig. 4.

In the schematic there is a time-delay switch which is used to eliminate outside control on the car. This is important because it gives the advantage of surprise when a burglary is being committed. The approximate one-minute time delay allows you to enter the car and shut the alarm off. This is enough time to shut the device off if you know how, but not enough if you don't. This stops the burglar from removing anything that is fastened inside the car or searching the interior. The schematic also shows that two switches are used in the driver's door. The second switch is used to activate the circuit with the time delay.

The on-off switch is a simple dpst switch placed somewhere in the middle of your ham gear. This way a burglar will never realize that it is the switch to deactivate the device. Also, the battery and siren are placed in the trunk. This makes it very hard for a burglar to disarm the system.

As noted in the schematic, there are four other switches marked "trunk," "hood" and "limit." These four switches are very important in deterring a person from stealing your car. The trunk and hood switches are simply placed in the trunk and hood, preventing anyone from opening either one and tampering with anything inside.



fig. 4. Simple burglar-proof auto alarm, All switches are shown as they would be when the doors, hood and trunk are closed.

The other two switches are harder to place, but they prevent the car from being moved. One of the switches is placed inside the car and is operated by the parking brake cable. Cutting the cable releases the tension on the cable and activates the alarm. The other switch is placed on one of the back shock absorbers. It is a limit switch, operating when the shock absorber is extended to its maximum. This sounds the alarm if the car is being towed away.

Installed correctly, this alarm system will keep your car well protected. It has already prevented three burglaries for me. Glenn Eisenbrandt, Jr.

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H ST-6

## It's all right here.

The HAL ST-6 terminal unit has been hailed by experienced RTTY amateurs. Its immunity to interference and noise is the talk of the RTTY world as the best in the business. In fact, we built it to highest standards — but kept the price in a range that you can afford.

The features of this unit tell the story of why it's so popular: Autostart operation, separate input filters for each shift, an antispace feature, and switch selection of 850 and 170 Hz shifts are standard. An extra discriminator for a 425 Hz shift is available as an option. A space-saving special power transformer is part of the package; it includes windings for low voltage and loop supplies, and a 115/230 VAC primary. Dual-in-line IC's are mounted in sockets for ease of testing and replacement. Seven G10 epoxy glass boards with reliable wiping contacts hold all circuitry. Tuning is read from a 1 ma. panel meter which, at the flick of a switch, serves as a loop current readout. Other visual indicators display AC power on, Mark, and Space conditions. Two other lamps indicate whether the ST-6 is in the receive or standby mode. For maximum safety, a three-wire grounding

cord and grounding outlet for the printer are included. The power supply card contains easy-toreplace clip-in fuses. The ST-6 is available factory assembled and aligned, or in kit form. The PC boards and cabinet only are also available.

A popular option designed to plug right in to the ST-6 is HAL's AK-1 AFSK oscillator. Available assembled or in kit form, the AK-1 is an AFSK oscillator that demonstrates stability and reliability. It provides switch selection of 170 Hz and 850 Hz shift using standard AFSK tones. The AK-1 may also be mounted in its own cabinet for use as an independent unit. Frequencies are set by 15turn trimmers for ease of accurate tone adjustment. The AK-1 operates on 12 VDC, or directly from the ST-6 power supply.

If you're ready for the very best RTTY at an attractive price, look into the HAL ST-6 TU, the 425 Hz discriminator, and the AK-1 AFSK oscillator. They'll give you all the help you need. Order yours today! Prices:

Assembled: / \$310 — ST-6 Terminal Unit \$350 — ST-6/425 Hz Disc. \$350 — ST-6/AK-1 \$390 — ST-6/425 Hz Disc/AK-1 Kit Form:

- \$147.50 ST-6 Terminal Unit \$ 35.00 - ST-6 Table or Rack Cabinet
- \$ 29.00 425 Hz Discriminator \$ 29.00 - AK-1 AFSK Unit

All prices postpaid, USA. For air shipment add \$4 for the ST-6 kit or cabinet, \$1 each for the 425 Hz kit or the AK-1 kit, \$10 for the assembled ST-6 with any options.



#### short circuits

#### universal tone encoder

A few transceiver models using diode PTT switching will not operate correctly with the Universal Tone Encoder shown in the July, 1975, issue. The problem occurs in the tone-burst mode after the PTT button is released, and results from the charging current drawn by C7. Some transceivers are not able to supply this current and will not return fully to the receive mode.



This problem is solved by adding CR2 and R27 as shown in the schematic above; the polarity of C7 was also reversed in the original schematic. The encoder will now operate with relay- and diode-switched transceivers. The new circuit board incorporates this change. Circuit boards are available from Larry McDavid, W6FUB, 185 South Alice Way, Anaheim, California 92806.

#### dc latch circuit

In the CMOS dc latch circuit, fig. 2, on page 44 of the August, 1975 issue, the D input of U2A (pin 5) should be connected to the  $\overline{\Omega}$  output (pin 2), not to the  $\Omega$  output (pin 1) as shown.

#### low-frequency loop antenna

In the article on the loop antenna receiving aid in the May, 1975 issue, no ground return is shown for the fet preamp (fig. 3) or Q multiplier (fig. 4). In both cases the 100k resistor connected to the gate of the HEP802 fet should be grounded.

#### automatic az/el control

Several errors appeared in the automatic azimuth/elevation rotator control system published in the January, 1975, issue of ham radio. In the base diagram for the 558 op amp (fig. 3), the inverting and non-inverting inputs to the lower op-amp are reversed (pin 5 should go to the non-inverting [+] input). In fig. 7 the sensed position output should be connected to the junction of the 100- and 750-ohm resistors, not to the op-amp output terminal. Also, add two to all IC numbers in the second column on page 29 and the first column on page 31 (U11C, for example, should be U13C).

Some readers have found that the frequency-selective amplifier in fig. 4 oscillates. This can be easily solved by increasing the value of the shunt resistance of the bridged-T network. In amplifier U1, for example, the resistor to change is the 7500-ohm unit connected between the two  $0.05 \,\mu$ F capacitors.

To eliminate difficulty with rf interference, shunt each rotator motor winding lead with a 0.01  $\mu$ F disc capacitor at the control unit case. Treat the leads to the rotator potentiometer as illustrated in fig. 1, shown here. In addition, the grounded end of the rotator potentiometer should be fastened to the circuit ground near the comparator, U11. Otherwise, unrelated ground currents may upset the sensed rotator position.



fig. 1. Use the circuit shown here with rotator potentiometer leads to eliminate difficulty with rf interference.

#### phase modulation techniques

In the article on phase modulation principles and techniques on page 28 of the July, 1975 issue, the value of R in fig. 7 should be 10k. The loss formula shown in fig. 7 should be

$$loss = 20 \log \left( \frac{X_C}{\sqrt{R^2 + X_C^2}} \right) dB$$

#### communications receiver

In the communications receiver described in the October, 1975 issue (page 32), the KVG XF9E crystal filter has 12 kHz bandwidth, not 2.4 kHz. Transformers T1 (fig. 2) and T1, T2 and T3 (fig. 8) are wideband transformers which 15TDJ wound on Ferroxcube 0.25" (6.5mm) diameter toroid cores (permeability of 1000 or more). The Amidon T50-6 cores specified in the article have low permeability and lowfrequency performance is poor. For those who have asked, Q6 in fig. 8 which is specified as an HEP S0014 may be replaced with a 2N3866 or 2N4427.

Designer I5TDJ has heard from several amateurs who have built duplicates of this receiver that they sometimes have trouble with the fet crystal oscillator circuits (fig. 8). He subsequently tested a number of fets and found that some circuits would not oscillate with fets with high  $I_{DSS}$  because of the large voltage drop across the 1000-ohm drain resistor which biased the fet into the pinch-off region. This can be solved by using low  $I_{DSS}$  fets or by reducing the value of the drain resistor to 100 ohms.

#### radiation hazards

In the September editorial W1DTY made an error when calculating the power density at 10 watts input to a 30-foot dish. Since the 10 watts is essentially spread over the area of the dish in the near field (within one or two dish diameters), the power density at 10 watts input is 0.061 mW/cm<sup>2</sup>. An input of 1642 watts would be required to reach 10 mW/cm<sup>2</sup>.

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Units are brand new. Complete satisfaction is guaranteed. If for any reason you are not completely satisfied, just return the undamaged unit within ten days for refund.





## logarithmic speech processor

New from MFJ Enterprises is the LSP-520BX speech processor, which provides 400% more rf power to your phone signal. The LSP-520BX adds this extra punch by means of three active filters, two of which are switch-selectable, and a low-distortion IC logarithmic amplifier with a 30-dB dynamic range, assuring constant transmitter output without clipping or appreciable distortion. Voice frequencies are tailored to put communication intelligence where it will do the most good — in your transmitted signal.

Four techniques are used to maximize the voice-to-noise power ratio. First, an rf-protected preamp is optimized for low-noise performance by using a premium, low-noise transistor. Second, putting two high-pass active filters *before* the log amplifier input ensures a clean, noise-free signal at the log amp output. Third, battery operation eliminates hum, and fourth, a filtered and shielded input circuit provides immunity from rf fields.

The low-noise preamp has a gain of about 43 dB. An emitter follower matches the preamp output to a 500-Hz two-pole active filter, which has a rolloff of 12 dB/octave (at 250 Hz the signal is attenuated 12 dB). A switchselectable two-pole 1400-Hz highpass active filter, which also has a 12-dB/ octave rolloff, follows the 500-Hz filter. When these two filters are cascaded, rolloff is 24 dB/octave below 500 Hz for maximum filtering. Following the two filters are a compression-level control and the logarithmic amplifier. A sixpole, low-pass active filter accepts the log amp output. This filter features steep rolloff at 36 dB/octave, with a 2100-Hz cutoff frequency. Thus, bandwidth restriction prevents a wide ssb signal and removes distortion products.

Installation is simple. Plug your microphone into the processor, plug the processor output into your transmitter microphone output, and you're ready for some pleasant surprises on the crowded phone bands. The LSP-520BX is priced at \$49.95 or \$35.95 in kit form. Write MFJ Enterprises, P.O. Box 494, Mississippi State, Mississippi 39762, or use *check-off* on page 142.

#### 525-MHz uhf prescaler

The new Pagel model 525 uhf prescaler divides frequency by ten to extend the range of any 50 MHz or higher counter to the vhf and uhf bands. The unit also contains a 20 dB preamp for the unscaled 1 MHz to 50 MHz range to improve frequency counter sensitivity to 5 millivolts rms or better. Sensitivity is 50 mV rms at 500 MHz, and 30 mV rms below 400 MHz. A through-line feature with an internal signal sampler can be used with transmitters up to 100 watts (requires 50-ohm dummy load). This feature can be used to perform simultaneous power and frequency measurements and is a great time saver.

The model 525 operates from the 117 Vac line or battery power (8 to 15 volts) may be used for portable or mobile use. Price is \$159. For more information, write to Pagel Electronics, 6742-C Tampa Avenue, Reseda, California 91335, or use *check-off* on page 142.

#### hamtronics catalog

Hamtronics, Inc., long known for its vhf preamplifiers and fm communications receiver kits for amateur and monitor applications, recently announced a new catalog, which is available to readers in return for a self-addressed, stamped envelope. It lists many new products, including a high performance version of its famous standard vhf preamp. This kit, which is wired in series with the coaxial antenna lead of vhf communications receivers of various operating frequencies, boosts the receive signal by 20 dB or more, depending on the frequency. It operates from +12 Vdc, and is constructed on a PC board. Cost of the kit is \$9 (wired and tested. \$14).

The second new product is a twostage grounded-gate preamplifier for uhf receivers in the 400-500 MHz range, including amateur, commercial, and monitor receivers. It provides 20 dB gain, and is priced at \$15 (kit) or \$30 (wired and tested). A companion uhf converter kit is available for operation on various i-f frequencies, thereby converting a vhf receiver into a uhf receiver. The converter kit is priced at \$20 plus crystal.

A new improved vhf receiver for fm communications has also been introduced in this catalog. It consists of a vhf converter board and a i-f/audio board. The converter is also available separately

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- \* 53 Keys
- \* One Chip MOS Encoder
- \* Upper and Lower Case
- \* Standard ASCII Output
- \* Two Key Lockout

We are happy to announce a new addition to our keyboard and encoder line. Our new KBD-3 uses a one chip MOS encoder system to give you maximum possible features with a minimum number of parts.

This keyboard produces a standard ASCII coded output that is compatible with TTL, DTL, RTL and MOS logic systems. You have the option of wiring the kit for normal typewriter style output in both upper and lower case letter, or all upper case format. All common machine control commands such as "line feed", "return", "control", etc. are provided on the keyboard. Four uncommitted or extra keys are available for your specific use requirements. Two of these have isolated output lines to the connector for special functions such as "here is<sup>R</sup>.

Keyswitches are standard, full travel style with gold plated contacts for long troublefree service. Requires +5 Volts and -12 Volts.

KBD-3 Keyboard and Encoder Kit \$49.50 ppd

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Whenever and wherever there's news in amateur Radio you can bet that HR REPORT is right there in the middle of it insuring that our readers are the best informed amateurs anywhere.

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to operate with various i-f frequencies. The vhf receiver kit is \$65 less crystal. A uhf version, which includes the uhf and vhf converters and i-f/audio board, is priced at \$80, less crystals.

For your free copy of this new catalog, send a self-addressed, stamped envelope to Hamtronics, Inc., 182 Belmont Road, Rochester, New York 14612.

#### **CW** filter



Operators active in contest and DX work will welcome a novel CW filter offered by Palomar Engineers, The circuit combines a wideband and narrowband filter to provide simulated stereo reception. Active filters prevent annoying ringing and give sharp skirt selectivity, which removes all signals except those within an 80-Hz bandwidth. The simulated stereo technique allows offfrequency signals to be heard, but because of the action of mind and ears, the off-frequency signals do not interfere with the desired signal.

The filter connects between your receiver and a set of stereo headphones. In the simulated-stereo mode, the narrowband signal is applied to one side of the stereo headset and the wideband signal to the other. Alternatively, the narrowphones by panel-switch selection. The simulated stereo mode uses both filters with a dramatic improvement over either filter alone. The desired signal is heard in both phones; the off-frequency signals and noise are heard in only one phone. The mind concentrates on the desired signal and rejects the interference — yet off-frequency calls can still be heard, which otherwise might be missed.

The center frequency of the CW filter is 800 Hz. Bandwidths of the narrow- and wide-band filters are 80 and 300 Hz respectively. A 9-volt transistor battery supplies power. Input impedance is 1 megohm; the output will drive either low- or high-impedance headphones. The panel switch has four positions: off (receiver output direct to phones); wideband amplifier to both phones: narrowband amplifier to both phones; and simulated stereo. The CW filter is \$39.95 postpaid in U.S. and Canada. More information may be obtained from Palomar Engineers, Box 455, Escondido, California 92025, or use check-off on page 142.

#### unique ic op-amp applications

A specialist in IC operational amplifiers, Walter Jung, has written this book on the uses of unique op amps. Unique op amps are those with characteristics that set them apart from previous amplifiers. Modified types of op amps are discussed along with totally unique types, such as programmable op amps, operational transconductance amplifiers, and quad current-differencing amplifiers. The material has been extracted from another Sams book, IC Op-Amp Cookbook. Heavily illustrated. 144 pages, softbound, \$4.95 from Ham Radio Books, Greenville, New Hampshire 03048.





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This magazine covers the whole Amateur Radio scene in Great Britain offering both a wide range of technical information and a description of many activities both on and off the air.

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#### To: Radio Communication Greenville, NH 03048

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#### **Regency crystal deck**



Topeka FM Communications has just introduced a new improved version of their highly popular 6T-HR2 six-channel crystal deck. Mounted in a Regency HR-2 or HR2-A, the deck allows full 12-channel transmit/receive capability. Improvements include a smaller board which makes installation notably easier. Component placement has been changed to allow netting without removing the speaker from the radio.

The new version, designated the 6T-HR2-3, is now available for \$15.50. Kit versions are also available for \$11.50. For more information, write or call Topeka FM Communications, Inc., 125 Jackson, Topeka, Kansas, 66603.

#### noise in electronics

Why is noise important? What is shot noise? How can noise figure be measured using a signal generator? These and dozens of other pertinent questions are answered in this new book for the amateur, engineer and technician. They provide the reader with a basic understanding of noise characteristics and noise measurement techniques for practical applications.

The author first introduces the reader to noise with explanations on white, pink, man-made, atmospheric and galactic noise. The remainder of the book answers questions about thermal noise, shot noise, noise bandwidth, special considerations for noise, signalto-noise ratio, noise figure and other miscellaneous noise characteristics.

Here's an opportunity to learn about flicker noise, noise power, the effect a-m detectors have on noise and dozens of other noise-related subjects. Easy-tounderstand answers are detailed without the complex mathematical manipulations usually required with noise associated calculations. Illustrations, examples, and tables of solutions are provided to further explain the answers. 96 pages, softbound, \$3.95 from HR Books, Greenville, New Hampshire 03048.

#### multicoupler/ preamplifier



The new multicoupler set from Radiation Devices features an antennalocated preamplifier and provides preamplification of signals at the base of a broadband high-frequency antenna to overcome coaxial cable loss. Preamplifier BBA-1/PMS-3 has greater than 9 dB gain over the band from 2 to 50 MHz. It receives power via the coaxial cable connecting it to the Multicoupler/Power Adapter Unit MPU-1. The MPU-1 provides four isolated signal ports to receivers or other equipment. Intermodulation and cross-modulation distortion products are greater than 60 dB below the desired signal at zero dBm output level. The unit operates from 115 Vac, 50 to 400 Hz.

For more information, contact Radiation Devices Company, Post Office Box 8450, Baltimore, Maryland 21234, or use *check-off* on page 142.

Telephones for XMAS "DECO-TEL" complete, ready to plug in. CRADLEPHONES CADDLEFHONES Red Brocade White & Gold Brocade Green & Gold Brocade Blue & White Cameo Any one of the above for only \$49.95 each. CANDLESTICK PHONES HOT LINE RED \$39,95 each. TRENDLINE TELEPHONE SETS with touch pad, desk or wall less ringer, new only \$34.95 each. Available in red, white, black, turquoise, each. Available in red, white, black, turquoise, blue & orange. TRENDLINE ROTARY DIAL less ringer, re-furbished only \$27.50 each. Colors as above. STANDARD DESK PHONE type 2500 with touch pad available in red, green and black, less ringer, new \$26.95 each. DESK PHONE type 500 or 80 rotary dial available in yellow, green, grey. Less ringer, new \$14.95 each. Checked out, less ringer, used \$8.95 each. WALL PHONES type 554 or 90 rotary dial \$8.95 each. WALL PHONES type 554 or 90 rotary dial available in beige, orange, yellow, red, blue, black, less ringer, new \$14.95 SPACE MAKER WALL PHONE rotary dial. Available in turquoise, black, beige, white. Less ringer, new \$17.50 each. Less ringer, used \$12.50 each. ringer, new \$17.50 each. Less ringer, used
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#### wind direction and velocity meter



Knowing wind speed and direction will allow you to trim that big beam antenna for minimum wind resistance when the next storm arrives. The model 75C Brunswick Wind Set by TMAC Products consists of a wind-speed transmitter, wind-direction transmitter, an indicator mounted in a handsome console, and all cables and mounting hardware. The transmitter units are low profile; the entire assembly measures only 12-3/4 inches high by 24 inches long (53 by 61cm) and may be mounted on any convenient surface.

The wind-speed transmitter consists of a dc generator coupled to a 5½-inch (14cm) diameter, spherical cup rotor assembly mounted on a 1-inch (2.5cm) diameter pvc pipe support. Wind speed is indicated by a 6-inch (15cm) diameter, 250-degree linear taut band pivot and jewel movement. Readout is in mph, with 1-mph divisions between 0 and 100 mph inscribed in white against a contrasting background.

The wind-direction transmitter uses hermetically sealed reed switches actuated by a magnet in an environmentprotected, low-friction assembly. Wind direction is indicated by eight panel lamps, one at each cardinal compass point, located around the periphery of the wind-speed indicator. Intercardinal



compass points are indicated by the illumination of two adjacent lamps. Thus, 16 compass points may be indicated; at least one indicator lamp will be on at all times. The instrument is powered by 110 V, 60-Hz. Price and additional information are available from TMAC Products, P.O. Box 28341 (Lincoln Village Branch), Columbus, Ohio 43228, or use *check-off* on page 142.

#### miniature touch-tone encoders

Data Signal has announced a new line of solid-state crystal-controlled Touch-Tone encoders which use a CMOS encoder IC. Only ¼ inch (6.5mm) thick, these self-contained units provide Touch-Tone capability to repeater stations or provide data entry. They are designed to be mounted directly on the side of hand-held portables, on the front of mobile transceivers, or on the dashboard of vehicles. The circuitry is completely rf proof, and all electronics are contained within the keyboard. Keyboards with 12 Touch-Tone digits are available in three sizes: 2¼x3 inches (57x76mm), 1½x2 inches (38x51mm) and 2x1½ inches (51x38mm). The 16-digit keyboard is 2 inches (51mm) square. These keyboard encoders, type DTM, require only three external connections and are priced at \$49.95.

Also available from Data Signal is a sub-miniature Touch-Tone encoder and keyboard which is designed for use with

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27-450 MHz Continuous Frequency Coverage

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hand-held fm transceivers. The encoder PC board measures a mere 0.8 by 1.2 inch (20x30.5mm) and is easily installed inside hand-held transceivers. The keyboard is available in the same four styles mentioned above and can be mounted on the side of the transceiver. The Touch-Tone encoder and keyboard, type SME, is priced at \$29.95.

In addition to the DTM and SME keyboards and encoders, the major components are also available for amateurs who want to build their own. The keyboard, choice of four styles, is \$8.50. The digital Touch-Tone encoder with 1-MHz HC-6/U crystal is \$12.50 (encoder with *slim* 1-MHz crystal is \$13.50). The miniature printed-circuit board is \$2.50. If you purchase a keyboard, encoder and crystal, the PC board, and all resistors and capacitors are provided free of charge.

For more information, write to Data Signal, Inc., 2212 Palmyra Road, Albany, Georgia 31701 or use *check-off* on page 142.

#### dual-trace oscilloscope adapter

A new RCA dual-tracer adapter that can be attached to any triggered or recurrent-sweep oscilloscope to update it to dual trace operation is now available.

The RCA WM-541A *Dual-Tracer* Adapter provides two displays on a single-trace oscilloscope for simultaneous viewing of two signals. Applications of the new RCA instrument include comparison tests of gain, frequency, response, distortion, phase shift, and time delay. In addition, the WM-541A can also be-used to add additional traces to dual-trace oscilloscopes.

Display modes included in the operation of the instrument are channel A only, channel B only, or both A and B channels simultaneously (chopped or alternate). The switching rate is continuously variable over a range designed to minimize flicker and beat interference.

The RCA WM-541A has additional features which include ac or dc coupling and vertical position controls for both channels; separate, variable sync-level control with polarity reversing switch; a zener-regulated power supply and LED power-on indicator. The inputs and outputs are terminated with BNC connectors for connection to the oscilloscope The latest cos/mos integrated circuitry is used for high performance operation. The instrument can be used from dc to 10 MHz.

The RCA WM-541A Dual-Tracer Adapter is priced at \$108.00. An optional WG-400A Direct/Low Capacitance Probe and Cable is available for \$15.00.

Additional information on RCA Electronic Instruments is available from RCA Distributor and Special Products Division, 2000 Clements Bridge Road, Deptford, New Jersey 08096, or use *check-off* on page 142.

#### corrosion-resistant vhf antenna

Most mobile antennas include a stainless-steel whip but here is one that is built entirely of stainless steel, brass, and an elastomer compound. This unit has been developed to meet and overcome two significant obstacles to antenna performance – corrosion and the necessity for a ground plane. The construction materials allow this popular model to live happily in a salt environment. The design has no need for a ground plane; this feature allows this unit to operate perfectly on a wood deck or fiberglass trunk lid.

For further details on this high gain, almost indestructible antenna, write to Gam Electronics, Inc., 191 Varney Street, Manchester, N.H. 03102, or use *check-off* on page 142.





#### synthesized scanning monitor



The new Bearcat 101 is a totally synthesized, five-band scanning monitor featuring a re-programmable custom integrated circuit. In addition to receiving the low (30-50 MHz), high (148-174 MHz) and uhf (450-470 MHz) bands, the unit will also receive the two-meter ham band (146-148 MHz) as well as uhf frequencies from 416 to 450 MHz.

The nerve center of the Bearcat 101 is provided by two exclusive, custom, large-scale ICs: one for *scanning* and the second for a non-volatile *memory* system. With the memory chip, the radio retains all frequencies programmed without the need for a battery. This feature allows users to order sets fully programmed with frequencies and assures program retention, even if the unit is unplugged or if there is a power outage.

The Bearcat 101 scans 16 channels. Individual lock-out switches are provided for each channel; these are also used in programming frequencies. Channel indicators are light-emitting diodes, providing a scan rate in excess of 20 channels-per-second. Selective Scan Delay, a new feature, permits the listener to remain on a channel for one second longer, in case of a reply on a simplex channel. The Bearcat Selective Scan Delay system permits delay on just those channels desired. Sensitivity in the low and high bands is measured at 0.6  $\mu$ V;
on the uhf bands, it typically ranges from 0.6 to 0.9  $\mu$ V. A six-pole crystal filter offers 70 dB of i-f selectivity.

For more information, write to the Electra Company, Cumberland, Indiana 46229, or use *check-off* on page 142.

## precision low-noise op amp

It isn't often that a precision, low noise, ultra-stable, high gain operation amplifier is put into production, and when one is, the cost is usually very high. Not so with a new state-of-the-art amplifier developed by National Semiconductor. Called the LH0044, the new operational amplifier includes all of these features plus low cost.

The LH0044 precision operational amplifier is intended to replace modules and chopper-stabilized monolithic amplifiers and is particularly well-suited for differential mode, inverting, and noninverting mode applications that require very low initial offset, low offset drift, very high gain and high power supply rejection ratio. In addition, the low initial offset and offset drift of the LH0044 eliminate costly and timeconsuming null adjustments.

Specifications include an input offset voltage less than 25 microvolts, long term stability better than  $\pm 1$  microvolt per month, a maximum offset drift of only 0.5 microvolts/°C, and a noise level lower than 0.7 microvolts peak-to-peak from 0.1 to 10 hertz. Other performance features include a CMRR and PSRR of 120 dB minimum, open-loop gain greater than 120 dB, and a common mode range wider than  $\pm 13$  volts. The power supply range is from  $\pm 2$  volts to  $\pm 20$  volts.

For more information, write to National Semiconductor Corporation, 2900 Semiconductor Drive, Santa Clara, California 95051, or use *check-off* on page 142.



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## 3000-volt silicon rectifiers



Electronic Devices has announced the development of a miniaturized, high voltage, high current silicon rectifier diode with a surge capacity of 300 amperes. The rectifier is an axial lead type. Electrical specifications for the series 3W3 diode are 3000 peak reverse voltage, 2 amp rating with 300 amp surge capacity. Two other similar designs are available with peak reverse voltages of 2000 and 2500 volts. Fast recovery types are also available. The exceptionally high surge capability and small size of these rectifiers results from a special diffusion process and larger junction with lower forward voltage drop.

For complete information, write to the Sales Manager, Electronic Devices, Inc., 21 Gray Oaks Avenue, Yonkers, New York 10710, or use *check-off* on page 142.

### tool catalog

A free tool catalog describing over 2500 individual items is offered by Jensen Tools and Alloys. "Tools for Electronic Assembly and Precision Mechanics" is a 112-page handbook of particular interest to amateurs, electronic technicians, engineers, scientists, and instrument mechanics working on fine assemblies. Section headings include screwdrivers, wrenches, pliers, tweezers, files, shears, knives, microtools, relay tools, power tools, metalworking tools, wire strippers, soldering equipment, lighting and optical equipment, work holders, test equipment, engineering and drafting supplies and electronic chemicals. New sections include metric tools, books, and wire wrapping tools. A 15-page tool kit section features the world famous Jensen kits for field engineers and kit builders.

Another important feature of the catalog is the inclusion of four pages of technical data on tool selection. These pages include sections on screwdriver selection, machine screw data, tool materials, metal conducitivity, color coding, wire and insulation data, solderability of metals, temperature conversion, drill sizes, metal gauges, metric conversion and safety. Five pages of "Tool Terms" are also included.

A free copy of the Jensen catalog may be obtained by writing to Jensen Tools and Alloys, 4117 North 44th Street, Phoenix, Arizona 85018, or by using *check-off* on page 142.

### contact cement



Industrial strength Zipbond contact cement bonds most materials almost instantly. It is easy to use, with no pre-mixing necessary, and is used directly from the squeeze applicator bottle (production-line dispenser also available). No heat or pressure treatment is needed, and Zipbond sets up quickly at room temperature.

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ical, as one drop covers a 1 inch square area to form a colorless transparent bond. For more information write to Instrument Division, Tescom Corporation, 2600 Niagara Lane North, Minneapolis, Minnesota 55441, or use *checkoff* on page 142.

### audio power amplifier

A new 40-watt (20 watt rms) B high-fidelity amplifier with total harmonic distortion of 0.2 per cent at 15 watts output is now available from Plainview Electronic Supply. This class B, quasi-complimentary amplifier is capable of delivering full output power into a standard 8-ohm speaker with a 500 mV input signal. Supply voltage can be +36 volts or  $\pm 18$  volts. Frequency response is from dc to 80 kHz.

The hybrid amplifier is designed for use in communications, stereo, public address and intercom systems, and is priced at \$10.65 in small quantities. For more information, write to Bernard Erde, Marketing Manager, Plainview Electronic Supply, 7 Gordon Avenue, Plainview, New York 11803, or use check-off on page 142.

### transformer catalog

Triad's new Catalog of Transformers, Inductors, Power Supplies and Circuit Cards, is now available. The 52-page catalog covers more than 30 categories of transformers, including autoformers, bridging, driver, input, interstage line matching and voltage correction. The inductor section of the catalog lists audio and filter reactors, high Q reactors, tone control and toroidal inductors.

These components are available from 44 Triad-Utrad representatives and distributors worldwide. Catalog requests should be addressed to Steve Fisher. General Manager, Triad-Utrad Distributor Services, 305 N. Briant Street, Huntington, Indiana 46750, or use *check-off* on page 142.

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TTP - TOUCH TONE PAD

XF1 - 10.7 MONOLITHIC

CRYSTALS: TX OR RX

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## FEATURES 1402 SM | 1405 SM

6 Channel Operation	• 6 Channel O
Individual Trimmers	<ul> <li>Individual T</li> </ul>
on all TX/RX Crystals	on all TX/R
All Crystals Plug In.	All Crystals
12 KHz Ceramic	<ul> <li>12 KHz Cera</li> </ul>
Filter	Filter
10.7 IF and	• 10.7 and 45
455 KC IF	KC IF
.3 Microvolt	<ul> <li>.3 Microvolt</li> </ul>
Sensitivity for 20 dB	Sensitivity f
Quieting	Quieting
Weight: 1 lb. 14 oz.	• Weight: 1 lb
less Battery	less Battery
S-Meter/Battery	Battery Indi
Indicator	• Size: 8 7/8
Size: 8 7/8 x 1 7/8	x 2 7/8
x 2 7/8	<ul> <li>Switchable</li> </ul>
2.5 Watts Minimum	Watts Minin
Output @ 12 VDC	Output @ 1
Current Drain RX	<ul> <li>Current Dra</li> </ul>
14 MA TX 500 MA	14 MA TX 4
Microswitch Mike	(Iw) 900 M/
Button	<ul> <li>Microswitch</li> </ul>
	Button
	- Habroakabl

•

#### rimmers X Crystals

- amic
- 5
- or 20 dB
- x 1 3/4
- 1 & 5 num
- in: RX 400 MA A (5W) Mike

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SM2 @ \$24.95 TE1 @ \$34.95	(SPECIFY FRED	OUENCY )
TTP @ \$44.95 XF1 @ \$8.95 EQUIP TRANSCEIVER AS FOLLOWS: XTALS A.	TX XTALS @ 146,52/52	\$3.00 eaRX XTALS @ \$3.00 ea B
C D	E	F
ENCLOSED IS		K MONEY ORDER MC BAC
CARD #	EXPIRAT	TION DATE
NAME		
ADDRESS		
CITY	STATE	ZIP
SIGNATURE		
SHIPPING AND HANDLING SALE VALID DECEMBER 1 - 31, 1975	PREPAID FOR C	HRISTMAS SPECIAL NEVADA RESIDENTS ADD SALES TAX



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			and the second second second second	and the second state of the second states		<ul> <li>A second sec second second sec</li></ul>

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In either a 5 volt TTL or a 9 volt C-MOS version this new module type IC keyer can be easily adapted to your own custom package or equipment.

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We have just gotten in a limited supply of H \$125.00 + IF SANTA DOESN'T TAKE THE SEE YOU AT MONTHLY SPECIAL LIST AVAILABLE WANTED: Good used FM & test equipment. No quant	Ai Band Rail Road Motracs 12VDC operable 2 Frequency Narrow Band Less Accs shipping E HINT SAROC LE SEND S.A.S.E. tity too large or small. Finders fee too.
We have just gotten in a limited supply of H \$125.00 + IF SANTA DOESN'T TAKE THE SEE YOU AT MONTHLY SPECIAL LIST AVAILABLE WANTED: Good used FM & test equipment. No quant	Ai Band Rail Road Motracs 12VDC operable 2 Frequency Narrow Band Less Accs shipping E HINT SAROC LE SEND S.A.S.E. tity too large or small. Finders fee too.
We have just gotten in a limited supply of H we have just gotten in a limited supply of H we have just gotten in a limited supply of H with the supply of H with the supply of H we have just gotten in a limited supply of H with the supply of H with the supply of H we have just gotten in a limited supply of H with the supply of H we have just gotten in a limited supply of H with the supply of H we have just gotten in a limited supply of H with the supply of H we have just gotten in a limited supply of H we hav	Ai Band Rail Road Motracs 12VDC operable 2 Frequency Narrow Band Less Accs shipping <b>HINT SAROC</b> LE SEND S.A.S.E. tity too large or small. Finders fee too. STORE HOURS: Mon-Thurs 9:30-6:00, Fri. 9:30-800 Sat. 9:30-3:00, Closed Sun. & Holidays.

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004022	1.75	CD4066	1.12	74C163	3 00	molarity digital unitmater in a kit form it
004023	25	CD4069	45	74C164	3 25	polarity digital voltimeter, in a kit form, it
CD4074	1.50	CD4071	45	74C173	2.60	reatures several options not available in any
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	THE KILOBYTE RAM CARD Per Kit \$49.9 "Complete 1Xx8 Memory * High Nous Immunity Components "Single 5v supply *500NS Access Time &Kit includes sockets, ICS & Board
The second	4 PDT SWITCHES, HIGH QUALITY P B. TYPES .69
	KITS EXAR ICS XR-2206KA SPECIAL \$17.95 Includes monolithic function generator IC, PC board, and assembly instruction manual.
-art A	XR-2206K8 SPECIAL \$27.95 Same as XR-2206KA above and includes external components for PC hoard.
GENERAL DESCRIPTION \$39.99 Per Kit	TIMERS         STEREO DECODERS           XR.320P         1.55         XR.1310P         \$3.2           XR.320P         1.55         XR.1310EP         3.2           XR.556CP         1.85         XR.1310EP         3.2           XR.556CP         3.20         WAVEFORM GENERATORS         3.2           XR.256CP         3.20         WAVEFORM GENERATORS         8.4           PHASE LOCKED LOOPS         XR.2206CP         \$PECIAL         4.8           XR.210         5.20         XR.220CP         \$4.20           XR.215         6.60         MISCELLANEOUS         XR.211CP         5.7           XR.2567CP         1.95         XR.2211CP         6.7         1.7           XR.82567CP         2.99         XR.2261         1.7         1.7
The JE801 is a three and one half digit, auto polarity digital voltmeter, in a kit form. It features several options not available in any commercial digital voltmeter. Its low cost is single plus and minus fifteen volt. Unregulated	*Special Requested Items*

single plus and minus fiftere volt, unregulated Rest power supply. The unit has a small size of three inches width, three and three quarters of an inch length, and one and a quarter inch height.

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A Free Sift ...

What do you do with junk equipment? Have you ever discarded equipment that just didn't do the job it was intended to do? Hams are noted for not discarding obsolete and worn out equipment; it goes to the junk box or gets traded at flea markets for something of greater use. However, the day finally comes when it becomes necessary to relegate the totally useless equipment to the burn pile.

A similar situation is presented to us in the Bible in the book of John 15:1-6. As long as we are useful to our heavenly Father we will be upgraded to become less obsolete and more useful. If the worn out equipment and junk in our ham shack had the same advantage we have as mentioned in Acts 16:31: "... Believe on the Lord Jesus Christ and thou shalt be saved . . . ", the burn pile would not be necessary. "If anyone separates from me (Jesus), he is thrown away like a useless branch, withers and is gathered into a pile with all the others and burned." John 15:6.

We have such a wonderful opportunity to be removed from the pile being readied for burning and put into service for God. "Sin pays its servants: the wage is death. But God gives to those who serve him: His free gift is eternal life through Christ Jesus our Lord." Rom. 6:23. Don't find yourself on that burn pile when you have no need to be. Take advantage of this free gift now for we don't know what day the Lord is coming. Turn from your way and give yourself to Jesus and receive this free gift.





Andy, Lee, Jane, Denny, Jan, Denny, Mary Jo and Clarissa









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# ham radio cumulative index 1968-1975

## antennas and transmission lines

#### general

Antenna control, automatic azimu	ith/	elev	ation	
WA3HLT		26	Jan	75
Correction	д	58,	Dec	75
Antenna dimension (HN)	·			
Antennas and capture area	p.	66,	Jun	70
кеміо	p.	42,	Nov	69
Antenna and control-link calculati repeater licensing	0115	for		
W7PUG	p.	58,	Nov	73
Antenna and feedline facts and fe	p.	59,	Dec	73
W5JJ	р.	24,	May	73
Antenna design, programmable				
W3DVO	n	70.	May	74
Antenna gain, measuring	μ.			
K6JYO Antenna switching solidistate	р	. 26	, Jul	69
W2EEY	<b>p</b> .	30,	Nov	68
Anti-QRM methods				
W3FQJ Bridge for antonne messurements	р.	50,	May	71
W2CTK	, ъ п.	34.	Sen	70
Cubical quad measurements	<b>P</b> .	,		
W4YM Dingle center insulator (HN)	p.	42,	Jan	69
WA1ABP	р.	69,	Mav	69
Diversity receiving system	r.			
W2EEY Dummy load and rf wattmotor	p.	12,	Dec	71
W2OLU	p.	56,	Apr	70
Dummy loads, experimental W8YFB	Б	36	Sen	68
Dummy load, low-power vhf	μ.		ocp	00
WB9DNI Effective radiated power (HN)	p.	40,	Sep	73
VE7CB	р.	72,	May	73
Feedpoint impedance characterist	ics		•	
of practical antennas	n	50	Dec	73
Filters, low-pass, for 10 and 15	μ.	50,	Dec	/3
W2EEY	р.	42,	Jan	72
WB8IFM	p.	54,	Nov	73
GDO, new uses for K2ZSQ	p.	48,	Dec	68
Grounding, safer (letter) WA5KTC	D.	59.	Mav	72
Ground rods (letter)	μ.	•••	may	
W7FS	p.	66,	Мау	71
Ground systems, vertical antenna W7LR	p.	30,	Мау	74
Headings, beam antenna W6FFC	p.	64.	Apr	71
Hoak, line 'n sinker (HN) WAANED		76	Son	68
Horizontal or vertical (HN)	μ.	70,	Seb	00
W7IV	p.	62,	Jun	72

Impedance measurements, non	reson	ant	ante	nna
Insulators, homemade antenna	(HN)	40,	Apr	74
W7ZC	р.	70,	May	73
Isotropic source and practical	anter	inas		
K6FD	р.	32,	May	70
Measurement techniques for an	itenna	IS		
and transmission lines	_	20		
Manauring antenna gain	p.	36,	may	74
Keivo		26	1	60
Mobile mount rigid (HN)	р	. 20	, Jui	03
VF7ARK	<b>_</b>	60	lan	73
Power in reflected waver	μ.	05,	Jan	13
Woods	n	٨Q	Oct	71
Reflected nower some reflection	, p.	4 <i>3</i> ,	001	/1
VE3AAZ	n	44	Mav	70
Reflectometers	μ.	,	may	/0
K1YZW	л.	65.	Dec	69
Rf current probe (HN)	<b>P</b> .	֥,		0-
W6HPH	p.	76.	Oct	68
Rf power meter, low-level		,		
W5WGF	p.	58,	Oct	72
Sampling network, rf - the mi	lli trap	>		
MEQIM	p.	34,	Jan	73
Smith chart, how to use				
WIDTY	р.	16,	Nov	70
Correction	р.	76,	Dec	71
Standing-wave ratios, importance	e of			
W2HB	р.	26,	Jul	73
Time domain reflectemental and	p.	67,	мау	/4
Avparimentar's approach	cuçai			
WAGPIA	~	22	May	71
T <sub>-</sub> R switch	μ.	۲٢,	way	/1
КЗКМО	n.	61	Anr	69
Voltage-probe antenna	μ.	·-,		
WIDTY	р.	20,	Oct	70

#### high-frequency antennas

All band antenna portable (HN)				
W2INS	p.	68,	Jun	70
All-band phased-vertical				
WA7GXO	р.	32,	May	72
Antenna, 3.5 MHz, for a small lot		~ ~		
W6AGX	р.	28,	Мау	73
W3EO I	~	54	May	72
Antenna systems for 80 and 40	p. mel	Prc	way	12
K6KA	D.	55.	Feb	70
Army loop antenna - revisited		,		
W3FQJ	p.	59,	Sep	71
Added notes	р.	64,	Jan	72
Beam antenna, improved triangu	lar	sha	ped	-
Ream for tan maters economica	р.	20,	мау	70
W1FPF	'n.	54.	Mar	70
Beverage antenna	μ.	,		
W3FQJ	p.	67,	Dec	71
Big beam for 10 meters				
VEITG	p.	32,	Mar	68
Bobtail curtain array, forty-meter				~~
VETTG Coaxial dibala multiband (HN)	р	. 58	, Jui	69
WARDK	n	71	May	73
Compact antennas for 20 meters	μ.	<i>,</i> <b>,</b>	way	/ 3
W4ROS	D.	38.	Mav	71
	μ.	,		

Converted-vee, 80 and 40 meter	
W6JKR Cubical quad antenna design pa	p. 18, Dec 69 arameters
Cubical-quad antennas, mechan	ical design of
Cubical-quad antennas, unusual	p. 44, Oct 74
WIDTY Cubical quad, three-band	р. 6, Мау 70
W1HXU Curtain antenna (HN)	p. 22, Jul 75
W4ATE Dipole, all-band tuned	p. 66, May 72
ZS6BT Dipole antennas on non-harmoi	p. 22, Oct 72
frequencies (HN) W2CTK	p. 72. Mar 69
Dipole beam W3FOJ	p. 56. Jun 74
Dipole pairs, low SWR	p. 42 Oct 72
Dipole sloping inverted-vee	p. 42, Oct 72
Double bi-square array	p. 46, Feb 03
Dual-band antennas, compact	p. 52, May 71
DX antenna, single-element	p. 16, Mar 70
Performance (letter)	p. 52, Dec 72 p. 65, Oct 73
Folded mini-monopole antenna W6SAI	p. 32, May 68
Four-band wire antenna W3FQJ	p. 53, Aug 75
Ground-plane, multiband (HN) JA1QIY	p. 62, May 71
Groundplane, three-band LA1EI	p. 6. May 72
Correction Epotpote (letter)	p. 91, Dec 72 p. 65 Oct 72
High-frequency amateur antenn	as p 28 Apr 69
High-frequency diversity antenn	ias
Horizontal antennas, optimum h	eight for
W/LR Horizontal antennas, vertical rac	p. 40, Jun 74 liation patterns
WA9RQY Inverted-vee antenna (letter)	p. 58, May 74
WB6AQF Inverted-vee antenna, modified	p. 66, May 71
W2KTW Large vertical, 160 and 80 meter	p. 40, Oct 71
W7IV Log-periodic antenna, 14, 21 and	p. 8, May 75 1 28 MHz
W4AEO Log-periodic antennas 7-MHz	p. 18, Aug 73
W4AEO	p. 16, May 73
W4AEO	p. 30, Oct 74
method for	e 14 May 75
Log-periodic antennas, vertical	p. 14, May /5
monopole, 3.5 and 7.0 MHz W4AEO	p. 44, Sep 73
Log-periodic beams, improved (I W4AEO	etter) p. 74, May 75
Log-periodic beam, 15 and 20 m W4AEO	eters p. 6. May 74
Log periodic feeds (letter) W4AEO	p. 66. May 74
Log-periodic, three-band W4AFO	n 28 Sen 72
Long-wire multiband antenna	p. 20, 30p 72
Loop receiving antenna	p. 20, NUV 69
WZ IN O	
Correction	p. 66, May 75 p. 58, Dec 75

ec	69	Mobile antenna, helically wound ZE6JP	p.	40.	Dec	72
	70	Mono-loop antenna (HN)		70	San	69
of	7.0	Multiband dipoles for portable u	se.			
νcι	74	Phased array, electrically-controll	p. ed	12,	мау	70
ау	70	W5TRS Phased vertical array, four-elemer	p. it	52,	Мау	75
lul	75	W8HXR Ouad antenna, multiband	р.	24,	Мау	75
ay	72	DJ4VM Receiving antennas	p.	41,	Aug	69
lct	72	K6ZGQ Satellito antonna, simple (HN)	p.	56,	May	70
ar	69	WA6PXY	p.	59,	Feb	75
	74	radiators, how to design	ver	ucai		
	74	Simple antennas for 40 and 80	р.	34,	Мау	75
νCτ.	12	W5RUB Simple 1-, 2- and 3-band antenna	p. is	16,	Dec	72
eb	69	W9EGQ Sloping dipoles	p	. 54	, Juł	68
ау	71	W5RUB Performance (letter)	р. р.	19, 76.	Dec Mav	72 73
ar	70	Small-loop antennas	p.	75	May	72
ec	72 73	Stub bandswitched antennas	μ.	50,	ivia y	<i>, L</i>
	, <b>5</b>	Suitcase antenna, high-frequency	р	. 50	, , ,,,,,,,,,,,,,,,,,,,,,,,,,,,,,,,,,,,	69
ау	76	VK5BI Tailoring your antenna, how to	p.	61,	Мау	73
ug	/5	KH6HDM Three-band ground plane	p.	34,	May	73
ay	71	W6HPH Triangle antennas	p.	32.	Oct	68
ay ec	72 72	W3FQJ	p.	56,	Aug	71
ct	72	W6KIW	р.	58,	May	72
pr	69	Triangle antennas (letter) K4ZZV	p.	72,	Nov	71
ct	69	Triangle beams W3FOJ	D.	70.	Dec	71
มท	74	Unidirectional antenna for the low	N-ti	requ	ency	
ern: ay	s 74	GW3NJY	p.	61,	Jan	70
ay	71	W7LR	s p,	50,	Apr	74
r.t	71	Vertical antenna, low-band W4IYB	p	. 70	. Jul	72
	75	Vertical antenna, three-band W9BOE	n	44	Mav	74
ау	75	Vertical antennas, improving perfo	p. srm	ance	e of	74
Jg	/3	Vertical antennas, performance ch	ara	order acter	istics	
ay	73	W/LR Vertical beam antenna, 80 meter	р.	34,	Mar	/4
ct	74	VE1TG Vertical dipole, gamma-loop-fed	р.	26,	May	70
av	75	W6SAI Vertical for 80 meters, top-loaded	p.	19,	Мау	72
.,		W2MB	p.	20,	Sep	71
вþ	73	W40Q	p.	16,	Apr	73
ау	75	Vertical, top-loaded 80 meter VE1TG	p.	48,	Jun	69
ay	74	Vertical-tower antenna system W40Q	р.	56,	Мау	73
ау	74	Whips and loops as apartment and W2EEY	en p.	паs 80.	Mar	68
q	72	Windom antenna, four-band W4VUO	p	62	Jan	74
~		Correction (letter)	р. р.	74,	Sep	74
	75	W6QVI	p.	48,	Dec	73
₹y ec	75 75	K6HTM	р.	46,	May	74
iy	73	160 meters with 40-meter vertical W21MB	р.	34,	Oct	72

#### vhf antennas

Antennas for satellite communicat	ion	\$, 51	mple	74
Circularly-polarized ground-plane	р.	<b>2</b> 4,	way	74
antenna for satellite communic	atio	ns	Dee	74
Collinear antenna for two meters.	p. ni	28, ne∙el	emen	74 t
W6RJO	p.	12,	Мау	72
Collinear antenna (letter) W6SAI	n	70	Oct	71
Collinear array for two meters, 4-	elei	ment		
WB6KGF Collinear antenna, four element 4	р 40.	. 6, МН7	May	71
WA6HTP	р.	38,	May	73
Collinear, six meter	~	59	Nov	69
Corner reflector antenna, 432 MH	z <sup>p.</sup>	55,		
WA2FSQ Cubical guad, economy six-meter	р.	24,	Nov	71
W6DOR Ground plane 2-meter 0.7 wave	p	. 50,	Apr	69
W3WZA	p.	40,	Mar	69
Ground plane, portable vhf (HN) K9DHD	n.	71.	Mav	73
J-pole antenna for 6-meters	μ.	,		
K4SDY Log-periodic, vagi beam	p.	48,	Aug	68
KERIL, WESAI		p. 8	, Jul	69
Microwaye antenna. Low-cost	p.	68,	Feb	70
Кеніј	p.	52,	Nov	69
W1HCI	p.	54,	Sep	75
Mobile antenna, six-meter (HN) W4PS1	n	77.	Oct	70
Moonbounce antenna, practical 1	44.	MHZ		
K6HCP Parabolic reflector antennas	р.	52.	Мау	70
VKJATN	p,	12,	Мау	74
WA9HUV	g	20	May	75
	H.	20,	way	•••
Parabolic reflector gain	н. г	20, 50	iviay Iul	75
Parabolic reflector gain W2TQK Parabolic reflectors, finding the foo	н. p cal	28, 1. 50 lengi	, Jul th (HI	75 N)
Parabolic reflector gain W2TQK Parabolic reflectors, finding the foo WA4WDL Barabolic reflector, 16-foot home	p al p.	28, . 50 lengi 57, w	, Jul th (HI Mar	75 N) 74
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB610M	p al p. bre	28, 1. 50 lengi 57, w 5, 8,	, Jul th (HI Mar Aug	75 N) 74 69
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-N W3AED	p al p. bre /H	28, 1. 50 lengi 57, w 1. 8, z 20,	, Jul th (Hf Mar Aug Mav	75 N) 74 69 73
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-M W3AED Short circult	p. al p. bre MH: p. p.	28, 1. 50 lengi 57, w 20, 8, 20, 58,	, Jul th (HI Mar Aug May Dec	75 N) 74 69 73 73 73
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-M W3AED Short circuit Simple antennas, 144-MHz WA3NFW	P al p. bre MH: p. p.	28, 50, 57, w 57, 8, 20, 58, 30,	, Jul th (HI Mar Aug May Dec May	75 1) 74 69 73 73 73
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-M W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, sc	p. al p. bre MH: p. p. hlid	28, 50, 57, w 20, 58, 30, stat	, Jul th (HI Mar Aug May Dec May e	75 75 74 69 73 73 73 69
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-M W3AED Short circult Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN)	p. p. p. p. p. p. p. p. p. p. p.	28, 50, 57, w 58, 20, 58, 30, stat 48,	May th (Hi Mar Aug May Dec May e May	75 75 74 69 73 73 73 69
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB610M Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W6BLZ	p. al p. bre f. p. hid p. p.	28, 50, 57, W 58, 20, 58, 30, stati 48, 78,	, Jul th (Ht Mar Aug May Dec May e May Aug	75 75 74 69 73 73 73 69 68
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for W44WDL Parabolic reflector, 16-foot home W8610M Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W66LZ Two-meter fm antenna (HN)	p al bre fre fre fre fre fre fre fre fre fre f	28, 50, 57, w 58, 30, stat 48, 78, 64,	, Jul th (HI Mar Aug Dec May e May Aug May	75 775 74 69 73 73 73 69 68 71
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for W44WDL Parabolic reflector, 16-foot home W861OM Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K22SQ Two-meter antenna, simple (HN) W66LZ Two-meter mobile antennas W66LZ	pi al bref Hip pi hid pi pi	23, 50 leng 57, w b, 8, 8 20, 58, 30, stat 48, 78, 64, 76,	, Jul th (HI Mar Aug Dec May e May Aug May May	75 77 69 73 73 73 69 68 71 68
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for W44WDL Parabolic reflector, 16-foot home W861OM Quadyagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W6BLZ Two-meter mobile antennas W6BLZ Vertical antennas, truth about %-	p p p p p p p p p p p p p p	23, 50 lengs 57, w 20, 8, 20, 58, 30, stati 48, 78, 64, 76, yeles	, Jul th (HI Mar Aug Dec May e May Aug May May	75 74 69 73 73 73 69 68 71 68
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHZ WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W6BLZ Two-meter fm antenna (HN) WB6KYE Two-meter mobile antennas W6BLZ Vertical antennas, truth about %- KØDOK	pi in pi i i pi pi pi in pi pi pi pi pi pi pi pi pi pi pi pi pi p	23, 50, 1998 57, w 58, 20, 58, 30, 58, 30, 58, 48, 76, yeler 48, 54, 54, 54,	, Jul th (HI Mar Aug Dec May e May May May Jan	75 74 69 73 73 69 68 71 68 71 68 74 75
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHZ WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W6BLZ Two-meter fm antenna (HN) WB6KYE Two-meter mobile antennas W6BLZ Vertical antennas, truth about %- KØDOK	pice pice pice pice pice pice pice pice	23, 50, 57, w 57, w 58, 30, 58, 30, 58, 48, 78, 48, 76, yeler 48, 54, 54, 54, 54, 54, 54, 54, 54, 54, 54	, Juli th (Hi Mar Aug Dec May e May May Jan Nay	75 74 69 73 73 69 68 71 68 74 75 68 74 75 68
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHZ WA3NFW Switch, antenna for 2 meters, so K22SQ Two-meter antenna, simple (HN) W6BLZ Two-meter fm antenna (HN) WB6KYE Two-meter mobile antennas W6BLZ Vertical antennas, truth about %- K0DOK Added note (letter) Vhf antenna switching without refl K22SQ	pice fille pice pice pice pice pice pice pice pic	23, 50, 57, 57, w 58, 20, 58, 30, 58, 48, 64, 76, veler 48, 54, 54, 76, 76, 76, 76, 76, 76, 76, 76, 76, 76	May , Juli th (Hith Mar Aug May Dec May May May May May May May Sep	75 74 69 73 73 69 68 71 68 74 75 68
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHZ WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W6BLZ Two-meter fm antenna (HN) W6BLZ Two-meter mobile antennas W6BLZ Vertical antennas, truth about %- KØDOK Added note (letter) Vhf antenna switching without refl KZZSQ Whip, 5/8-wave, 144 MHZ (HN) VE3DDD	pice pice pice pice pice pice pice pice	23, 50 lengs 57, w 20, 8, 20, 58, 30, stat 48, 54, 76, yeler 48, 54, 76, 76, 76, 76, 70,	, Juli th (HI Mar Aug Dec May May May May Jan May Jan Sep Apr	75 74 69 73 73 73 69 73 73 69 68 71 68 74 75 68 73
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-N W3AED Short circult Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W6BLZ Two-meter mantenna (HN) W86KYE Two-meter mobile antennas W6BLZ Vertical antennas, truth about %- KØDOK Added note (letter) Vhip. 5/8-wave, 144 MHz (HN) VE3DDD Yagi, 1296-MHz W2CQH	r p p p p p p p p p p p p p	23, 50 leng 57, 57, 57, 57, 57, 57, 57, 57, 57, 58, 54, 58, 58, 58, 58, 58, 58, 54, 54, 54, 54, 54, 54, 54, 54, 54, 54	, Juli th (HI Mar Aug May Dec May Dec May May Jan Sep Apr May	75 74 69 73 73 69 68 71 68 74 68 73 68 73 72
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W6BLZ Two-meter fm antenna (HN) W86KYE Two-meter mobile antennas W6BLZ Vertical antennas, truth about %- KØDOK Added note (letter) Vhf antenna switching without refl K2ZSQ Whip, 5/8-wave, 144 MHz (HN) VE3DDD Yagi, 1296-MHz W2CQH 10-GHz dielectric antenna (HN)	pice pice pice pice pice pice pice pice	23, 50 leng 57, 58, 20, 58, 30, 58, 30, 58, 48, 78, 64, 76, 76, 76, 76, 76, 70, 24, 54, 70, 24, 50, 50, 50, 50, 50, 50, 50, 50, 50, 50	, Juli th (Mar Aug Dec May e May May Jan Sep Apr May	75 74 73 73 73 69 68 71 68 74 75 68 73 72 75 72 75
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W6BLZ Two-meter fm antenna (HN) W6BLZ Two-meter mobile antennas W6BLZ Vertical antennas, truth about %- KØDOK Added note (letter) Vhf antenna switching without refl K2ZSQ Whip, 5/8-wave, 144 MHz (HN) VE3DDD Yagi, 1296-MHz W2CQH 10-GHz dielectric antenna (HN) WA4WDL 144-MHz vertical, %-wavelength	n pilip pilip pi piwopingo pi pi	23, 50 leng 57, 58, 30, 58, 30, 58, 30, 58, 30, 58, 30, 58, 30, 58, 30, 58, 58, 30, 58, 58, 58, 58, 58, 58, 58, 58, 58, 58	May , Juli Mar Aug May Dec May May May May May May Jan Apr May May	75 75 74 69 73 73 69 68 71 68 74 75 68 73 72 75 73 73 73 73 73 73 73 73 73 73
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB610M Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W66LZ Ywo-meter fm antenna (HN) W66LZ Vertical antennas, truth about %- KØDOK Added note (letter) Vhf antenna switching without refl K2ZSQ Whip, 5/8-wave, 144 MHz (HN) VE3DDD Yagi, 1296-MHz W2CQH 10-GHz dielectric antenna (HN) WA4-MHz vertical, %-wavelength K6KLO	pi p	23, 50, 50, 50, 57, 57, 58, 30, 558, 30, 558, 30, 558, 564, 76, 5448, 54, 54, 54, 54, 54, 54, 54, 54, 54, 54	May , Juli Mar Aug May Dec May May May Jan May May May Jan May May Jan	75 77 73 73 69 73 73 69 68 71 68 73 72 75 74 75 74
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for W44WDL Parabolic reflector, 16-foot home W861OM Quadyagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K22SQ Two-meter antenna, simple (HN) W66LZ Vertical antennas, truth about %- KØDOK Added note (letter) Vhf antenna switching without refl K22SQ Whip, 5/8-wave, 144 MHz (HN) VE3DDD Yagi, 1296-MHz W2CQH 10-GHz dielectric antenna (HN) W44WDL 144-MHz vertical, %-wavelength built from CB mobile whip (HN) WHON	r sal breff b	23, 50 lengi 57, w 57, w 20, 58, 30, 58, 30, 58, 30, 58, 48, 48, 54, 48, 54, 76, 14, 76, 76, 24, 80, 40, 24, 80, 40, 54, 40, 54, 54, 54, 54, 54, 54, 54, 54, 54, 54	May , Juli Mar Aug May Dec May May May Jan May May Jan May Jan May Jan	75 75 74 69 73 73 69 68 71 68 75 68 73 72 75 74 75
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for W44WDL Parabolic reflector, 16-foot home W861OM Quadyagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K22SQ Two-meter antenna, simple (HN) W66LZ Vertical antennas, truth about %- KØDOK Added note (letter) Vhf antenna switching without refl K22SQ Whip, 5/8-wave, 144 MHz (HN) VE3DDD Yagi, 1296-MHz W2CQH 10-GHz dielectric antenna (HN) WA4WDL 144-MHz vertical, %-wavelength K6KLO 144-MHz antenna, %-wavelength built from CB mobile whip (HN) WB4WSU 432-MHz OSCAR antenna (HN)	n partine participation partic	23, 50 lengi 57, wy 57, wy 58, 30, 58, 30, 58, 30, 58, 48, 54, 76, 76, 54, 76, 54, 76, 76, 24, 80, 40, 76, 70, 24, 80, 40, 67, 67, 67, 67, 67, 67, 67, 67, 67, 67	, Juli th (HI Mar Aug May Dec May May Jun May Jun	75       75         74       69         73       73         69       73         73       69         73       69         73       69         73       69         73       69         73       69         68       71         68       73         72       75         74       74
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for W44WDL Parabolic reflector, 16-foot home W86IOM Quadyagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K22SQ Two-meter antenna, simple (HN) W66LZ Vertical antennas, truth about %- K0DOK Added note (letter) Vhf antenna switching without ref K22SQ Whip, 5/8-wave, 144 MHz (HN) VE3DDD Yagi, 1296-MHz W2CQH 10-GHz dielectric antenna (HN) WA4WDL 144-MHz vertical, %-wavelength K6KLO 144-MHz antenna, %-wavelength built from CB mobile whip (HN) W1JAA	r papertine pide pie pie pie pie pie pie pie pie pie pi	23, 50 lengt 57, 57, 57, 57, 57, 57, 57, 57, 57, 57,	, Juli th (HI Mar Aug May Dec May May May Jun May May Jun May Jun Jun	75       74         69       73         73       69         73       73         68       71         68       71         68       73         72       68         73       75         68       73         72       74         74       75
Parabolic reflector gain W2TQK Parabolic reflectors, finding the for WA4WDL Parabolic reflector, 16-foot home WB6IOM Quad-yagi arrays, 432- and 1296-N W3AED Short circuit Simple antennas, 144-MHz WA3NFW Switch, antenna for 2 meters, so K2ZSQ Two-meter antenna, simple (HN) W66LZ Two-meter mobile antennas W66LZ Two-meter mobile antennas W66LZ Vertical antennas, truth about %- KØDOK Added note (letter) Vhf antenna switching without ref K2ZSQ Whip, 5/8-wave, 144 MHz (HN) VE3DDD Yagi, 1296-MHz W2CQH 10-GHz dielectric antenna (HN) WA4WDL 144-MHz vertical, %-wavelength K6KLO 144-MHz antenna. %-wavelength built from CB mobile whip (HN) W1JAA 1296-MHz Yagi array W3AED	r paper the paid of particular pa	23, 25, 20, 25, 20, 25, 20, 25, 20, 25, 20, 25, 20, 25, 20, 25, 20, 25, 20, 25, 20, 25, 20, 25, 20, 20, 20, 20, 20, 20, 20, 20, 20, 20	, Juli the (Hit Mar Aug May Dec May May May May May May May May Jun May Jun May Jun May Jun May	75       73       69       73       73       69       73       73       68       71       68       72       74       74       75       74       75 <td< td=""></td<>

#### matching and tuning

Antenna coupler for three-band	beam	IS		
Antenna coupler, six-meter	p. 4	2,	мау	72
KIRAK Antenna impedance transformer	p. for	44,	Jul	71
receivers (HN) W6NIF	n	70	lan	70
Antenna matcher, one-man		 	lun	
Antenna tuner adjustment (HN)	р. 4	24,	Jun	/1
WA4MTH Antenna tuner, automatic	p. t	53,	Dec	75
WAØAQC Antenna tuner, medium-power tor	p. 3 oidal	36,	Nov	72
WB2ZSH Antenna tuner for optimum powe	p, { Pr tra	58, ans	Jan fer	74
W2WLR	p. 2	8,	May	70
W3FQJ	p. 5	58,	Dec	72
W3FQJ	p. !	58,	Jan	73
Balun, adjustable for yagi antenn W6SAI	as p. 1	4,	Мау	71
Balun, Simplified (HN) WAØKKC	р.	73,	Oct	69
Baluns, wideband bridge W6SAL WA6BAN	n 2	R	Dec	68
Broadband Antenna Baluns	p	с.	tun	20
Couplers, random-length antenna	р.	0,	Jun	
Gamma-match capacitor, remotel	р.3 у сог	32, ntre	Jan	70
K2BT Gamma-matching networks, how t	р.7 ode	4, sigi	May n	75
W7ITB	р. 4	6,	May	73
W8YFB	p.	6,	Мау	73
W6MUR	p. 4	6,	Nov	73
W7CSD	şignii p.	ng 58,	Jul	73
Loads, affect of mismatched tra W5JJ	nsmi p.€	ttei 50,	Sep	69
Matching, antenna, two-band with W6MUR	stub	)S 18.	Oct	73
Matching system, two-capacitor		:0	Son	72
Measuring complex impedance wi	th sw	ir t	oridge	
WB4KSS Mobile transmitter, loading	р. 4	6,	Мау	75
W4YB Noise bridge, antenna	р.4	6,	Мау	72
WB2EGZ Noise bridge, antenna (HN)	p. 1	8,	Dec	70
K8EEG Noise bridge for impedance meas	р. 7 шет	1, 1601	May	74
YA1GJM	p. 6	52,	Jan	73
Phase meter, rf	p. c	, v,	wer	75
Quadrifilar toroid (HN)	p. 2	28,	Apr	13
W9LL Stub-switched, stub-matched anti	p. 5 enna:	i2, s	Dec	75
W2EEY Swr alarm circuits	р. 3	34.	Jan	69
W2EEY Swr bridge	р, 7	73,	Apr	70
WB2ZSH	р, (	55,	Oct	71
W6DQB	p. 4	eα 0,	Мау	70
Swr bridge readings (HN) W6FPO	p. 6	з,	Aug	73
Swr meter W6VSV	р.	6,	Oct	70
Transmatch, five-to-one W7IV	р. 5	4,	Mav	74
Transmission lines, grid dipping W2OLU	(HN	) 12.	Feh	71
Transmission lines, uhf	_ , ,	 6	May	71
A A A A A A A A A A A A A A A A A A A	M - 2	41	un el X	**

#### towers and rotators

Antenna and rotator preventive i	mai	nten	ance	
WA1ABP	p.	66,	Jan	69
Antenna mast, build your own f	iiit-c	ver		
W6KRT	p.	42.	Feb	70
Correction	р.	76.	Sep	70
Az-el antenna mount for satellite				
communications				
W21 Y	n	34	Mar	75
Cornell Dubilior rotators (HN)	р.	34,	Wai	15
	_	01		75
NONA	р.	ō2,	way	/5
Keeping your beam, tips for		~ ~	-	~ ~
W6BLZ	_р.	50,	Aug	68
Pipe antenna masts, design data	for			
W3MR	р.	52,	Sep	74
Added design notes (letter)	p.	75,	May	75
Rotator, AR-22, fixing a sticky				
WAIABP	р.	34.	Jun	71
Rotator, T-45, Improvement (HN	)	,		
WAOVAM	'n	64	Sen	71
Stress analysis of antenna syste	me.	•••,	σσρ	
WOE71		22	Oct	71
Telesepping to mente (1161)	μ.	20,	001	<i>'</i>
relescoping to masts (HIN)	_	<b>6</b> 7	<b>-</b>	77
WAØRKC	р.	5/,	reo	13
Tiltover tower base, low-cost				
WAIABP	.р.	86,	Apr	68
Tilt-over tower uses extension lad	der			
W5TRS	р.	71,	May	75
Tower, homemade tilt-over				
WA3EWH	р.	28,	May	71
Tower, wind-protected crank-up				
(HN)	p.	74,	Oct	69
Wind loading on towers and anter	ına			
structures, how to calculate				
K4KI	n	16	Aug	74
Added note	μ. 	56	Int	75
Added note	P.	- 201	5 5 61	10

#### transmission lines

Coax cable dehumidifier				
K4RJ	р.	26,	Sep	73
Coax connectors, repairing broker	۱ (F	IN)		
WØHKF	p.	66,	Jun	70
Coaxial cable, checking (letter)		~~		-7.1
W2ULU Coaxial cable connectors (HN)	р.	68,	мау	11
WAIARP	n.	71	Mar	69
Coaxial-cable fittings, type-F	μ.	/ - /		0.5
K2MDO	р.	44,	May	71
Coaxial cable supports (HN)			-	
W2GA	p.	56,	Jun	68
Coaxial cable, what you know abo	out		_	
W9ISB	р.	30,	Sep	68
Coaxial feedthrough panel (HN)	_	70	A	~~
WOURE	p.	70,	Apr	69
WoVCI	nen	50	May	72
Coax Low-cost (HN)	μ.	50,	inay	12
K6BIJ	р.	74.	Oct	69
Coaxial transmission lines, under	grou	und		
WØFCH	р.	38,	May	70
Impedance transformer, non-sync	nro	nous	(HN)	)
W5TRS	р.	66,	Sep	75
Open-wire feedthrough insulator (	HN.	) <u> </u>	Maria	70
W4RINL	р.	79,	мау	/5
Single reedline for multiple ante	nna	50	May	71
Relate the second second second	р.	50,	way	11
WOLEY	'n	36	Anr	68
	ь,	30,	Apr	00
	-	70	Mar	60
Turner wall to wall antenna (HN)	μ.	12,	141G1	05
W2011Y	n	56	Dec	70
Ubf microstrin swir bridge	μ.	50,	60	,,,
WACGC	n	22	Dec	72
	μ.	~~,	000	12

## p. 70, Sep 72 audio

W45SN7 n 28 lun 71
Audio amplifier and squelch circuit
Audio CW filter
W7DI p. 54, Nov 71 Audio filter, tunable, for weak-signal
communications K6HCP p. 28, Nov 75
Audio filters, aligning (HN) W4ATE n. 72, Aug. 72
Audio filters, inexpensive
Audio filter mod (HN)
Audio module, a complete p. 60, Jan 72
K4DHC p. 18, Jun 73 Audio-oscillator module, Cordover
WB2GQY p. 44, Mar 71 Correction p. 80, Dec 71
Audio transducer (HN)
Binaural CW reception, synthesizer for
Compressor, dual channel
W2EEY p. 40, Jul 68 Distortion and splatter
K5LLI p. 44, Dec 70 Filter for CW, tunable audio
WA1JSM p. 34, Aug 70 Filter-frequency translator for cw reception,
integrated audio W2EEY p. 24. Jun 70
Filter, lowpass audio, simple
Filter, simple audio
Filter, tunable peak-notch audio
W2EEY p. 22, Mar 70 Filter, variable bandpass audio
W3AEX p. 36, Apr 70 Hang agc circuit for ssb and CW
WIERJ p. 50, Sep 72 Headphone cords (HN)
W2OLU p. 62, Nov 75
K6KA p. 34, Sep 68
W5JJ p. 67, Sep 73
W4AYV p. 66, Jul 72
Microphone preamplifier with agc Bryant p. 28, Nov 71
Microphone, using Shure 401A with the Drake TR-4 (HN)
G3XOM p. 68, Sep 73 Microphones, muting (HN)
W6IL p. 63, Nov 75 Notch filter tunable BC
WA5SNZ p. 16, Sep 75
W6GXN p. 50, Feb 73
WA1JSM p. 48, Sep 70
W8GRG p. 20, Jul 71
Pre-emphasis for ssb transmitters OH2CD p. 38, Feb 72
Rf clipper for the Collins S-line K6JYO p. 18, Aug 71
Rf speech processor, ssb W2MB p. 18, Sep 73
Speaker-driver module, IC WA2GCF p. 24, Sep 72
Speech amplifiers, curing distortion
Speech clipper, IC
Added notes (letter) p. 18, Feb 73

Speech clippers, rf				
G6XN p. 26, Nov;	р.	12,	Dec	72
Added notes p. 58, Aug 73;	р.	72,	Sep	74
Speech clipping in single-sideband	t eo	luipi	ment	
K1YZW	p.	22,	Feb	71
Speech clipping (letter)				
W3EJD	p.	72,	, Jul	72
Speech_processing				
W1DTY	p.	60,	Jun	68
Speech processing, principles of				_
ZL1BN	р.	28,	Feb	75
Added notes p. 75, May 75;	р.	64,	Nov	75
Speech processor for ssb, simple				
кбрнт	р.	22,	Apr	70
Speech processor, IC				
VK9GN	р.	31,	Dec	71
Speech processor, logarithmic				
WA3FIY	p.	38,	Jan	70
Squelch, audio-actuated			-	
K4MOG	р.	52,	Apr	72
Tape head cleaners (letter)		~~		
K4MSG	р.	62,	мау	12
Tape head cleaning (letter)				
Buchanan	р.	67,	Oct	72

## commercial equipment

Alliance rotator improvement (HN)				
K6JVE	р.	68,	May	72
Alliance T-45 rotator Improvement	'н	N)	-	
WA AVAM	È.	64	Sen	71
	μ.	07,	ocp	
CDR AR-22 rotator, fixing a sticky		~ •	1	71
WAIABP	р.	34,	Jun	11
Clegg 27B, S-meter for (HN)				
WA2YUD	р.	61,	Nov	74
Collins receivers 300-Hz crystal fil	ter	for		
WINTY	D	58.	Sen	75
Colling S line newer supply mod (h	111	<b>0</b> 0,	002	
Collins 3-line power supply filled (r		61	<b>)</b> )	71
WOIL		. 01	, Jui	/4
Collins S-line, reducing warm-up d	rift			
W6VFR	р.	46,	Jun	15
Collins S-line, rf clipper for				
K6JYO	р.	18,	Aug	71
Correction	р.	80,	Dec	71
Collins S-line spinner knob (HN)	-			
WEVER	n	69.	Apr	72
Colline S line transporter mod (UN	۰ <u>۳</u> .	<b>.</b> .,		
Collins 5-line transceiver mod (rin	<u>,</u>	71	Nov	72
	р.	/1,	NOV	12
Collins 325-3 audio (HN)		~ •	0.4	
Кока	р.	64,	Uct	/1
Collins 32S-1 CW modification (HN	)			
W1DTY	p.	82,	Dec	69
Correction	р.	76,	Sep	70
Collins 51J PTO restoration				
W6SAI	p.	36,	Dec	69
Collins 70K-2 PTO, correcting med	nan	lical		
backlash (HN)				
K9WEH	р.	58.	Feb	75
Collins 75A4 avc mod (letter)	·			
W9KNI	n	63.	Sen	75
Colline 7544 hints (HN)	μ.	00,	996	
WeVED	~	69	Anr	72
O IN TEM IN THE REAL PROVIN	μ.			12
Collins 75A4, increased selectivity	tor	(HI	N)	
WIDIY	р.	62,	NOV	15
Collins 75A-4 modifications (HN)				_
W4SD	р.	67,	Jan	71
Collins 75A4 PTO, making it perfor	m	like	new	
W3AFM	р.	24,	Dec	74
Collins 75A-4 receiver, improving of	ve	rloa	d	
response in				
W6ZO	n.	42.	Apr	70
Short circuit	n.	76.	Seo	70
Colling 75S frequency synthesizer	<b>P</b>	,		
W6NRI	r	8	Dec	75
Calling D2004 improving the and	<b>ب</b>	. 0, dat	2000	, ,
want want	uci	10	ector	74
	p.	. 12	, Jul	14
Collins R390A modifications				
WA2SUT	р.	58,	Nov	75

Comdel speech processor, increas versatility of (HN)	ing	the		
W6SAI Cornell-Dubilier rotators (HN)	р.	67,	Mar	71
K6KA Drake R-4 receiver frequency synthesizer for	р.	82,	May	75
W6NBI Modification (letter)	Р р.	. 6, 74,	Aug Sep	72 74
Drake R-4C, electronic bandpass t Horner	uni p.	ng i 58,	n Oct	73
microphone with (HN)	_	<i>c</i> 0	<b>C</b>	70
Drake W-4 directional wattmeter	р, _	68,	Sep	/3
Elmac chirp and drift (HN)	р.	<b>0</b> 0,	Mar	70
EX crystal and oscillator WB2EG7	р. ი	60, 60	Anr	68
Galaxy feedback (HN) WA5TFK	р. п.	71	lan	70
Hallicrafters HT-37, increased side suppression	eba	nd	5	
W3CM Hammarlund HQ215, adding 160-r	p. net	48, er	Nov	69
W2GHK Heath CA1. ten-minute timer from	р. (Н	32, N)	Jan	72
K8HZ Heath HG-10B vfo, independent ke	p. vin	74	Jul (HN	68 )
K4BRR Heath HM-2102 wattmeter, better	р.	67,	Sep	, 70
balancing (HN) VE6RF	D.	56.	Jan	75
Heath HM-2102 wattmeter mods ( K3VNR	ett	er) 64.	Sep	75
Heath HO-10 as RTTY monitor sco K9HVW	pe p.	(HŃ 70,	) Sep	74
Heath HW-7 mods, keying and rec blanking (HN)	eive	er	·	
WA5KPG Heath HW-12 on MARS (HN)	р.	60,	Dec	74
K8AUH Heath HW-16 keying (HN)	р.	63, 	Sep	71
W/DI Heath HW16, vfo operations for	р.	57,	Dec	73
Short circuit	р. р.	54, 58,	Dec	73 73
Heath HW-17A, perking up (HN)	p.	70,	Aug	70
WA5PWX Heath HW-100, HW-101, grid-curre	p. nt	66,	Mar	71
monitor for K4MFR	р.	46,	Feb	73
Heath HW-100 incremental tuning KIGUU	(H) p	N) 67,	Jun	69
Heath HW-100, the new W1NLB	р.	64,	Sep	68
Heath HW-100 tuning knob, loose VE3EPY	(Hf p.	۱) 68,	Jun	71
Heath HW-101, using with a separ receiver (HN)	ate			
WA1MKP Heath HW-202, adding private-line	p.	63,	Oct	73
WA8AWJ Heath IM-11 vtvm, convert to IC v	p. oltr	53, nete	Jun r	74
K6VCI Heath SB-100, using an outboard	p. rec	42, eive	Dec	74
with (HN) K4GMR	p.	68,	Feb	70
Heath SB102 modifications (HN) W2CNQ	p.	58,	Jun	75
Heath SB-102, rf speech processor W61VI	fo p.	r 38,	Jun	75
Heath SB-200 amplifier, modifying 8873 zero-bias triode W6UOV	fo p.	r the 32.	a Jan	71
Heath SB-200 amplifier, six-meter K1RAK	cor p.	vers 38,	sion Nov	71

Heath SB-300, RTTY with	_
Heath SB-303, 10-MHz coverage for (HN)	8
WIJE p. 61, Feb 7 Heath SB-400 and SB-401, improving alc	4
response in (HN) WA9FDQ p. 71, Jan 7	0
Heath SB-610 as RTTY monitor scope (HN) K9HVW p. 70, Sep 7	4
Heath SB-650 using with other receivers K2BYM p. 40, Jun 7	3
Heath SB receivers, RTTY reception with (HN) K9HVW p. 64, Oct 7	1
Heath SB-series crystal control and narrow shift RTTY with (HN)	-
WA4VYL p. 54, Jun 7	3
K6KA p. 75, Dec 7	1
WA6FNR p. 84, Dec 6	9
Heathkit, noise limiter for (HN) W7CKH p. 67, Mar 7	1
Heathkit HW202, fm channel scanner for W7BZ p. 41, Feb 7	5
James Research oscillator/monitor W1DTY p. 91, Mar 6	8
James Research permaflex key W1DTY p. 73, Dec 6	8
Kenwood TS-520 CW filter modification (HN) W7ZZ p. 21, Nov 7	5
Knight-kit inverter/charger review W1DTY p. 64. Apr 6	9
Knight-kit two-meter transceiver W1DTY p. 62, Jun 7	0
Mini-mitter II W6SLO p. 72 Dec 7	ĩ
Motorola channel elements	•
Motorola Dispatcher, converting to 12 volts	2
Short circuit p. 64, Mar 7	4
VE4RE p. 60, Aug 7	1
Motorola P-33 series, improving WB2AEB p. 34, Feb 7	1
Motorola receivers, op-amp relay for W6GDO p. 16, Jul 7	3
Motorola voice commander, improving WØDKU p. 70, Oct 7	0
Motrac Receivers (letter) K5ZBA p. 69, Jul 7	1
Quement circular slide rule W2DXH p. 62. Apr 6	8
Regency HR-2, narrowbanding WA8TMP p. 44, Dec 7	3
Regency HR-212, channel scanner for WA 0/S IK n 28 Mar 7	5
SBE linear implfier tips (HN) WA6DCW p. 71 Mar 6	ğ
SB301/401, Improved sidetone operation	å
Signal One review	, ,
Spurious causes (HN)	9
K6KA p. 66, Jan 7 Standard 826M, more power from (HN)	4
WB6KVF p. 68, Apr 7 Swan television interference: an	5
effective remedy W2OUX p. 46, Apr 7	1
Swan 120, converting to two meters K6RIL p. 8. May 6	8
Swan 350 CW monitor (HN)	2
Correction (letter) p. 77, May 7 Swap 350, receiver incremental turing (UN)	3
KIKXA p. 64, Jul 7	1
WB2MIC p. 67, Aug 6	9
swan 250, update your (HN) K8ZHZ p. 84, Dec 6	9

Telefax transceiver conversion		16	4	74
	. <b>р</b> .	10,	Apr	74
Ten-Tec Argonaut, accessory paci	kage	tor		
W7BBX	р.	26,	Apr	74
Ten-Tec RX10 communicators rec	eive:	r		
WINLB	р.	63,	Jun	71
T150A frequency stability (HN)	-			
WB2MCP	р.	70,	Apr	69
Yaesu sideband switching (HN)			•	
W2MUU	р.	56,	Dec	73
Yaesu spurious signals (HN)	•			
K6KA	p.	69,	Dec	71
Units affected (letter)	р.	67.	Oct	73
Yaesu FT101 clarifier (letter)	•			
K1NUN	р.	55,	Nov	75

### construction techniques

AC line cords (letter) W6EG	р.	80.	Dec	71
A dab of paint, a drop of wax (HN	٦. ١	78		68
Aluminum's new face	р. Б	60,	May	69
Aluminum tubing, clamping (HN)	μ.	00, 70	May	75
Antenna insulators, homemade (H	p. IN)	78,	мау	75
APC trimmer, adding shaft to (HN	р. I)	70,	мау	/3
W1ETT Blower-to-chassis adapter (HN)	Р	. 68	, Jul	69
K6JYO BNC connectors, mounting (HN)	р.	73,	Feb	71
W9KXJ Capacitors, oil-filled (HN)	р.	70,	Jan	70
W2OLU Center insulator dinale	р.	66,	Dec	72
WA1ABP	р.	69,	May	69
W3KBM	p.	61,	Nov	75
WA1ABP	p.	71,	Mar	69
Coax connectors, repairing broken WØHKF	ı (Н р.	IN) 66,	Jun	70
Coax relay coils, another use (HN KØVOY	) p.	72.	Aug	69
Cold galvanizing compound (HN) W5UNF	D.	70.	Sen	72
Color coding parts (HN)	р. п	58	Feb	72
Component marking (HN)	р. п	66	Nov	71
Deburring holes (HN)	μ.	75	1	/ I C 0
Drill guide (HN)	ρ	. 75,	Jui	
W5BVF Drilling aluminum (HN)	p.	68,	Oct	71
W61L Enclosures, homebrew custom	p.	67,	Sep	75
W4YUU Exploding diodes (HN)	р	. 50	, Jul	74
VE3FEZ Ferrite beads	p.	57,	Dec	73
W5JJ Files, cleaning (HN)	p.	48,	Oct	70
Walton	p.	66,	Jun	74
K10RV	p.	34,	Mar	73
WØKMF	p.	60,	Nov	68
VE3BUE	p.	77,	Oct	68
Grounding (HN) W9KXJ	р.	67.	Jun	69
Heat sinks, homemade (HN) WAØWOZ	р.	69.	Sep	70
Homebrew art WØPEM	<b>D</b> .	56	Jun	69

Hot etching (HN)				
K8EKG Hot wire stripper (HN)	p.	66,	Jan	73
W8DWT IC lead former (HN)	р.	67,	Nov	71
W5ICV	p.	67,	Jan	74
W3WLX	р.	26,	Sep	75
VE3BUE	ни) р.	76,	Sep	68
Magnetic fields and the 7360 (HN W7DI	l) p.	66,	Sep	73
Metric conversions for screw and W1DTY	iw b .q	ires 67,	izes Sep	75
Miniature sockets (HN)	n.	84	Dec	69
Minibox, cutting down to size (HN	)	57	Mar	71
Mobile installation, putting togeth	er	37,	Aum	(7 (0
WØFCH Mobile mount bracket (HN)	р.	36,	Aug	69
W4NJF Modular converter, 144-MHz	p.	70,	Feb	70
W6UOV Neutralizing tip (HN)	p.	64,	Oct	70
ZE6JP Noisy fans (HN)	p.	69,	Dec	72
W8IUF	p.	70, 67	Nov	72
Nuvistor heat sinks (HN)	μ.	67, 57	000	75
WAØKKC Parasitic suppressor (HN)	ρ.	57,	Dec	/3
WA9JMY Printed-circuit boards, cleaning (F	p. IN)	80,	Apr	70
W5BVF Printed-circuit boards, how to ma	p. ke	66,	Mar	71
K4EEU Printed circuit boards low-cost	p.	58,	Apr	73
W6CMQ	p.	44,	Aug	71
WAYER	-	16	1	75
	р.	10,	Jan	/ 5
Printed-circuit boards, practical photofabrication of	р.	10,	Jan	
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN)	p. P	. 6,	Sep	71
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN)	p. p. p.	. 6, 76,	Sep Oct	71 70
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W6JVE	p. p p. p.	. 6, 76, 58,	Sep Oct Apr	71 70 74
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W6JVE Printed-circuit tool (HN) W2GZ	р. р. р.	10, . 6, 76, 58, 74,	Sep Oct Apr May	71 70 74 73
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit tool (HN) W2GZ Printed circuits without printing W4ZG	р, р р, р, р,	10, . 6, 76, 58, 74, 62,	Sep Oct Apr May Nov	71 70 74 73 70
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit tool (HN) W2GZ Printed circuits without printing W4ZG Professional look, for that VE3GFN	р. р. р. р. р.	10, . 6, 76, 58, 74, 62, 74,	Sep Oct Apr May Nov Mar	71 70 74 73 70 68
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W6JVE Printed-circuit tool (HN) W2GZ Printed circuits without printing W4ZG Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM	р. р. р. р. р. р.	10, . 6, 76, 58, 74, 62, 74, 57,	Sep Oct Apr May Nov Mar Jun	71 70 74 73 70 68 68
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit tool (HN) W2GZ Printed circuits without printing W4ZG Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction	p, p, p, p, p, p,	10, . 6, 76, 58, 74, 62, 74, 57,	Sep Oct Apr May Nov Mar Jun	71 70 74 73 70 68 68 68
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit tool (HN) W2GZ Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction W7OE Rack construction, a new approace	p. p. p. p. p. p. p.	<ol> <li>6,</li> <li>6,</li> <li>76,</li> <li>58,</li> <li>74,</li> <li>62,</li> <li>74,</li> <li>57,</li> <li>48,</li> <li>55</li> </ol>	Sep Oct Apr May Nov Mar Jun	71 70 74 73 70 68 68 68
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W6JVE Printed-circuit tool (HN) W2GZ Printed circuits without printing W4ZG Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction W7OE Rack construction, a new approact K1EUJ Rectifier terminal strip (HN)	p. p. p. p. p. p. p. p.	<ol> <li>6,</li> <li>76,</li> <li>58,</li> <li>74,</li> <li>62,</li> <li>74,</li> <li>57,</li> <li>48,</li> <li>36,</li> </ol>	Sep Oct Apr May Nov Mar Jun Jun Mar	71 70 74 73 70 68 68 68 68 70
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Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit tool (HN) W2GZ Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction W7OE Rack construction, a new approad K1EUJ Rectifier terminal strip (HN) W5PKK Restoring panel lettering (HN) W8CL Screwdriver adjustment (HN)	p p p p p p p p p p p p p p p p p	<ol> <li>6,</li> <li>76,</li> <li>58,</li> <li>74,</li> <li>62,</li> <li>74,</li> <li>57,</li> <li>48,</li> <li>36,</li> <li>80,</li> <li>69,</li> </ol>	San Sep Oct Apr May Nov Mar Jun Jun Mar Apr Jan	<ul> <li>71</li> <li>70</li> <li>74</li> <li>73</li> <li>70</li> <li>68</li> <li>68</li> <li>68</li> <li>70</li> <li>70</li> <li>73</li> </ul>
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit tool (HN) W2GZ Printed circuits without printing W4ZG Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction W7OE Rack construction, a new approad K1EUJ Rectifier terminal strip (HN) W5PKK Restoring panel lettering (HN) W8CL Screwdriver, adjustment (HN) WAØKGS	p. p. p. p. p. p. p. p. p. p. p. p.	<ol> <li>6,</li> <li>6,</li> <li>76,</li> <li>58,</li> <li>74,</li> <li>62,</li> <li>74,</li> <li>57,</li> <li>48,</li> <li>36,</li> <li>80,</li> <li>69,</li> <li>66,</li> </ol>	Sep Oct Apr May Nov Mar Jun Jun Mar Apr Jan Jan	<ul> <li>71</li> <li>70</li> <li>74</li> <li>73</li> <li>70</li> <li>68</li> <li>68</li> <li>68</li> <li>68</li> <li>70</li> <li>70</li> <li>73</li> <li>71</li> </ul>
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Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit tool (HN) W2GZ Printed circuits without printing W4ZG Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction W70E Rack construction, a new approad K1EUJ Rectifier terminal strip (HN) W5PKK Restoring panel lettering (HN) W8CL Screwdriver, adjustment (HN) WAØKGS Silver plating for the amateur W4KAE Small parts tray (HN) W2GA	p P P P P P P P P P P P P P P P P P P P	<ol> <li>6,</li> <li>6,</li> <li>76,</li> <li>58,</li> <li>74,</li> <li>62,</li> <li>74,</li> <li>57,</li> <li>48,</li> <li>36,</li> <li>80,</li> <li>69,</li> <li>66,</li> <li>62,</li> <li>58,</li> </ol>	Sep Oct Apr May Nov Mar Jun Jun Jun Jan Jan Jec Jun	71 70 74 73 70 68 68 68 70 70 73 71 68 68
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit standards (HN) W2GZ Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction W7DE Rack construction, a new approad K1EUJ Rectifier terminal strip (HN) W5PKK Restoring panel lettering (HN) W8CL Screwdriver, adjustment (HN) WAØKGS Silver plating for the amateur W4KAE Small parts tray (HN) W2GA Solder dispenser, simple (HN)	p p p p p p p p p p p p p p p p p p p	<ol> <li>6,</li> <li>6,</li> <li>76,</li> <li>58,</li> <li>74,</li> <li>62,</li> <li>74,</li> <li>57,</li> <li>48,</li> <li>36,</li> <li>69,</li> <li>66,</li> <li>62,</li> <li>58,</li> <li>76,</li> </ol>	Sep Oct Apr May Nov Mar Jun Jun Jan Jan Dec Jun Sep	71 70 74 73 70 68 68 68 68 70 70 73 71 68 68 68 68
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit tool (HN) W2GZ Printed circuits without printing W4ZG Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction W7OE Rack construction, a new approad K1EUJ Rectifier terminal strip (HN) W5PKK Restoring panel lettering (HN) W5PKK Restoring panel lettering (HN) W8CGS Silver plating for the amateur W4KAE Small parts tray (HN) W2GA Solder dispenser, simple (HN) W2KID Soldering aluminum (HN) ZE6JP	p p p p p p p p p p p p p p p p p p p	<ol> <li>6,</li> <li>6,</li> <li>76,</li> <li>58,</li> <li>74,</li> <li>62,</li> <li>74,</li> <li>57,</li> <li>48,</li> <li>36,</li> <li>69,</li> <li>66,</li> <li>62,</li> <li>58,</li> <li>76,</li> <li>67.</li> </ol>	Sep Oct Apr May Nov Mar Jun Jun Jun Jan Jan Jan Jan Sep Mav	71 70 74 73 70 68 68 68 68 70 70 73 71 68 68 68 68 72
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit tool (HN) W2GZ Printed circuits without printing W4ZG Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction W70E Rack construction, a new approad K1EUJ Rectifier terminal strip (HN) W5PKK Restoring panel lettering (HN) W8CL Screwdriver, adjustment (HN) W8CS Silver plating for the amateur W4KAE Small parts tray (HN) W2GA Solder dispenser, simple (HN) W2KID Soldering aluminum (HN) ZEGJP Soldering fluxes (HN)	p p p p p p p p p p p p p p p p p p p	10, 6, 76, 58, 74, 62, 74, 57, 48, 36, 69, 66, 62, 58, 76, 57, 57	Sep Oct Apr May Nov Mar Jun Jun Jun Jan Jan Jec Jun Sep May	71 70 74 73 70 68 68 68 70 70 73 71 68 68 68 68 72 68
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit tool (HN) W2GZ Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction W7DE Rack construction, a new approad K1EUJ Rectifier terminal strip (HN) W5PKK Restoring panel lettering (HN) W8CL Screwdriver, adjustment (HN) W4/KGS Silver plating for the amateur W4KAE Small parts tray (HN) W2GA Solder dispenser, simple (HN) W2KID Soldering aluminum (HN) ZEGJP Soldering fluxes (HN) K3HNP Soldering tip (HN)	p p p p p p p p p p p p p p p p p p p	10, 6, 76, 76, 74, 62, 74, 62, 74, 66, 66, 62, 58, 76, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 67, 57, 57, 57, 57, 57, 57, 57, 57, 57, 5	Sep Oct Apr May Nov Mar Jun Jun Jan Jan Dec Jun Sep May Jun	71 70 74 73 70 68 68 68 70 73 71 68 68 68 68 72 68 72 68
Printed-circuit boards, practical photofabrication of Hutchinson Printed-circuit labels (HN) WA4WDK Printed-circuit standards (HN) W5JVE Printed-circuit standards (HN) W2GZ Professional look, for that VE3GFN Punching aluminum panels (HN) W7DIM Rack and panel construction W7DE Rack construction, a new approad K1EUJ Rectifier terminal strip (HN) W5PKK Restoring panel lettering (HN) W8CL Screwdriver, adjustment (HN) WAØKGS Silver plating for the amateur W4KAE Small parts tray (HN) W2GA Solder dispenser, simple (HN) W2KID Soldering aluminum (HN) ZE6JP Soldering fluxes (HN) K3HNP Soldering tip (HN) Lawyer	F P P P P P P P P P P P P P P P P P P P	10, 6, 76, 76, 58, 74, 62, 74, 57, 48, 36, 69, 66, 62, 58, 76, 57, 68, 57, 68, 57, 68, 57, 68, 57, 68, 57, 76, 57, 68, 57, 57, 68, 57, 57, 57, 58, 58, 58, 58, 58, 58, 58, 58, 58, 58	Sep Oct Apr May Nov Mar Jun Jun Mar Jun Jan Dec Jun Sep May Jun Feb	71 70 74 73 70 68 68 68 68 68 70 70 73 71 68 68 68 72 68 70

Tilt your rig (HN)				
WA4NED	p.	58,	Jun	68
Toroids, plug-in (HN)				
K8EEG	p.	60,	Jan	72
Transformers, repairing		~ ~	••	
W6NIF	р.	66,	Mar	69
WELLIC	_	76	Nou	60
libf coax connectors (HN)	р.	70,	NUV	69
WØLCP	Ð.	70.	Sen	72
Uhf hardware (HN)	۲.	,		•
W6CMQ	p.	76,	Oct	70
Underwriter's knot (HN)				
WIDTY	р.	69,	May	69
Vectorbord tool (HN)		-		-
WAIKWJ	р.	70,	Apr	12
would	TIX D	62	Ν) Διιστ	74
Watercooling the 2039	μ.	02,	VuR	/4
K6MYC	n.	30.	Jun	69
Wiring and grounding		,	,	
WIEZT	р.	44,	Jun	69
Workbench, electronic				
W1EZT	р.	50,	Oct	70

### features and fiction

Alarm, burglar-proof (HN)		56	Dec	75
Pipeling 1970 issues of here radie	νμ. VL	1NI)	Dec	/5
W1DHZ	р.	72,	Feb	71
Brass pounding on wheels	·			
K6QD	p.	58,	Mar	75
Dynistor, the				
W6GXN	р.	49,	Apr	68
Catalina wireless, 1902				
W6BLZ	р.	32,	Apr	70
Early wireless stations		~ .	<u>.</u> .	~~
W6BLZ	p.	64,	Oct	68
Electronic bugging				
K2ZSQ	р.	70,	Jan	68
Fire protection in the ham shack				_
Darr	p.	54,	Jan	71
First wireless in Alaska				
W6BLZ	р.	48,	Apr	73
Ham Radio sweepstakes winners,	197	72		
WINLB	p.	. 58,	յու	72
Ham Radio sweepstakes winners,	197	73		
WINLB	p	. 68,	Jul	73
Ham Radio sweepstakes winners,	197	'5		
WINLB	p	. 54,	Jul	75
How to be DX				
W4NXD	р.	58,	Aug	68
Nostalgia with a vengeance				
W6HDM	p.	28,	Apr	72
QSL return, statistics on				
WB6IUH	р.	50,	Dec	68
Photographic illustrations				
WA4GNW	р.	72,	Dec	69
Reminisces of old-time radio				
K4NW	р.	40,	Арг	71
Secret society, the				
W4NXD	р.	82,	May	68
Use your old magazines				
Foster	р.	52,	Jan	70
What is it?				
WA1ABP	p.	84,	May	68
Wireless Point Loma				
W6BLZ	р.	54,	Apr	69

### fm and repeaters

Amateur wht the operation				
W6AYZ	ρ.	36,	Jun	68
Antenna and control-link calcula	tions	;		
for repeater licensing				
W7PUG	р.	58,	Nov	73
Short circuit	p.	59,	Dec	73
Antennas, simple, for two-meter	fm			
WA3NFW	р.	30,	May	73

Antenna, two-meter fm (HN) WB6KYE	D.	64.	Mav	71
Antenna, 5%-wavelength, two-mete K6KLO	r n	40	Jul	74
Antenna, 5% wavelength two-meter	, N		,	, ,
WB4WSU Audio amplifier and squelch unit	р.	67,	Jun	74
W6AJF	p.	36,	Aug	6 <b>8</b>
to open repeaters	_	22		74
Autopatch system for vhf fm repea	μ. ate	rs	war	74
Base station, two-meter fm	p	. 32. 	, Jui	74
W9JTQ Carrier-operated relay	р.	22,	Aug	73
KØPHF, WAØUZO Carrier-operated relay and call mo	p. nit	58, or	NOV	72
VE4RE Cavity filter, 144-MHz	p.	22,	Jun	71
WISNN Channel scanner	р.	22,	Dec	73
W2FPP Channels, three from two (HN)	p.	29,	Aug	/1
VE7ABK Charger, fet-controlled for nicad ba	p. atte	68, eries	Jun	71
WAØJYK Collinear antenna for two meters,	p. nir	46, ne⊷	Aug	75
element W6RJO	p.	12,	Мау	72
Collinear array for two meters, 4-e WB6KGF	ler p.	nent . 6,	Мау	71
Continuous tuning for fm converte W1DHZ	rs p.	(HN 54,	) Dec	70
Control head, customizing VE7ABK	p.	28,	Apr	71
Deviation measurement (letter) K5ZBA	р.	68,	May	71
Deviation measurements W3FOJ	р.	52,	Feb	72
Deviation meter (HN) VE7ABK	p.	58,	Dec	70
Digital touch-tone encoder for vhf W7FBB	fm p.	28,	Apr	75
Discriminator, quartz crystal WAØJYK	р.	67.	Oct	75
Distortion in fm systems W5JJ	р.	26,	Aug	60
Encoder, combined digital and bui K8AUH	rst p.	48.	Aug	69
Filter, 455-kHz for fm WAØJYK	р.	22,	Mar	72
Fm demodulator, TTL W3FQJ	р.	66,	Nov	72
Fm receiver frequency control (let W3AFN	ter) p.	) 65,	Apr	71
Fm techniques and practices for v W6SAI	hf p	ama . 8,	iteurs Sep	69
Short circuit Fm transmitter, solid-state two-me	p. ter	79,	Jun	70
W6AJF Em transmitter Sonobaby 2 mete	P	. 14	, Jul	71
WAØUZO Short Circuit	م	96. 8,	Oct Dec	71 71
Crystal deck for Sonobaby	р.	26,	Oct	72
W4JAZ Short circuit	р.	40, 72	Jan	71
Frequency synthesizer, inexpensiv	e.	14,	Λþi	/1
WØOA	p.	50, 65	Aug	73 74
Frequency-synthesizer, one-crystal	μ.	00,	2011	,4
WØMV	p.	30,	Sep	73
Frequency synthesizer, for two-me WB4FPK	ter p	tm . 34	Jul	73
ldentifier, programmable repeater W6AYZ	р.	18,	Apr	69
Short circuit	р	. 76	Jul	69

I-f system, multimode	<b>.</b>	71
Indicator, sensitive rf	Sep	/1
Interface problems, fm equipment (HN)	Apr	73
MODPY p. 58, Interference, scanning receiver (HN)	Jun	/5
K2YAH p. 70, Logic oscillator for multi-channel	Sep	72
WISNN p. 46,	Jun	73
Wobile antenna, magnet-mount W1HCI p. 54,	Sep	75
Mobile operation with the Touch-Tone pad WØLPO p. 58,	Aug	72
Correction p. 90,	Dec	72
Modulation standards for vhf fm	Арг	73
Monitor receivers, two-meter fm	Jun	
WB5EMI p. 34, Motorola channel elements	Apr	74
WB4NEX p. 32, Motorola fm receiver mods (HN)	Dec	72
VE4RE p. 60, Motorola P-33 series, improving the	Aug	71
WB2AEB p. 34, Meterola voice commander improving	Feb	71
WØDKU p. 70,	Oct	70
K5ZBA p. 69,	Jul	71
Narrow-band fm system, using ICs in W6AJF p. 30,	Oct	68
Phase-locked loop, tunable, 28 and 50 MHz W1KNI p 40	lan	73
Phase modulation principles and techniqu	es	75
VE2BEN p. 28, Correction p. 59,	Jul Dec	75 75
Power amplifier, rf 220-MHz fm K7JUE p. 6,	Sep	73
Power amplifier, rf, 144 MHz Hatchett p. 6,	Dec	73
Power amplifier, rf, 144-MHz fm W4CGC p. 6,	Apr	73
Power amplifier, two-meter fm, 10-watt W1DTY p. 67,	Jan	74
fm equipment		
Preamplifier, two-meter	Jun	/3
WA2GCF p. 25, Preamplifier, two meter	Mar	12
W8BBB p. 36, Private-line, adding to Heath HW-202	Jun	74
WA8AWJ p. 53, Push-to-talk for Styleline telephones	Jun	74
W1DRP p. 18, Receiver alignment techniques whf fm	Dec	71
K41PV p. 14,	Aug	75
multichannel fm	<b>c.</b> h	- 4
Receiver for two meter, fm	reb	74
W9SEK p. 22, Short circuit p. 72,	Sep Apr	70 71
Receiver isolation, fm repeater (HN) W1DTY p. 54,	Dec	70
Receiver, modular fm communications K8AUH p. 32,	Jun	69
Correction p. 71, Receiver, modular, for two-meter fm	Jan	70
Added notes p. 42,	Feb Jul	72 72
WA2GBF p. 42, Added notes p. 73, Receiver performance, comparison of	Feb Jul	72
WA2GBF p. 42, Added notes p. 73, Receiver performance, comparison of VE7ABK p. 68, Receiver, tunable vhf fm	Feb Jul Aug	72 72 72
WA2GBF p. 42, Added notes p. 73, Receiver performance, comparison of VETABK p. 68, Receiver, tunable vhf fm K8AUH p. 34, Receiver, vhf fm	Feb Jul Aug Nov	72 72 72 71
WA2GBF p. 42, Added notes p. 73, Receiver performance, comparison of VE7ABK p. 68, Receiver, tunable vhf fm K8AUH p. 34, Receiver, vhf fm WA2GCF p. 6, Receiver, vhf fm	Feb Jul Aug Nov Nov	72 72 72 71 71

Receiver, Vht fm (letter)	_	76	May	72
Relay, operational-amplifier, for	μ.	70,	way	/5
Motorola receivers		16	Int	72
Repeater control with simple time	rs	. 10	, 501	
W2FPP Correction	р. п.	46, 91.	Sep Dec	72 72
Repeater decoder, multi-function				
Repeater installation	р.	24,	Jan	13
W2FPP Repeater problems	р.	24,	Jun	73
VE7ABK	P.	38,	Mar	71
Repeater, receiving system degrad K5ZBA	atı p.	оп 36,	Мау	69
Repeater transmitter, improving		24	Det	60
Repeaters, single-frequency fm	μ.	24,	OCI	
W2FPP Reset timer automatic	р.	40,	Nov	73
W5ZHV	p.	54,	Oct	74
WA4YAK	p.	64,	Oct	75
Scanner, vhf receiver		22	Feb	77
Scanning receiver, improved	μ.	****	100	
for vhf fmn WA2GCF	p.	26,	Nov	74
Scanning receiver modifications, vi	hf	fm so	Feb	74
Scanning receivers for two-meter f	p. m	00,	reo	14
K41PV Sequential encoder, mobile fm	р.	28,	Aug	74
พราวบ	φ.	34,	Sep	71
repeater control	ње			
W8GRG	p.	22,	วันส	71
W3FQJ	p.	62,	Apr	75
S-meter for Clegg 27B (HN)				
WA2YUD	р.	61,	Nov	74
WA2YUD Squelch-audio amplifier for	р.	61,	Nov	74
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU	р. р.	61, 68,	Nov Sep	74 74
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi wR4WSU	p. p. os	61, 68, 36,	Nov Sep Dec	74 74 75
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic	p. p. p.	61, 68, 36,	Nov Sep Dec	74 74 75
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØPHF, WAØUZO	p. p. p. p.	61, 68, 36, 44,	Nov Sep Dec	74 74 75 74
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØPHF, WAØUZO Test set for Motorola radios KØRKD	p. p. p. p.	61, 68, 36, 44, 12,	Nov Sep Dec Nov	74 74 75 74 73
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØPHF, WAØUZO Test set for Motorola radios KØBKD Short circuit	p. p. p. p. p.	61, 68, 36, 44, 12, 58,	Nov Sep Dec Nov Dec	74 74 75 74 73 73
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØPHF, WAØUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN)	p. p. p. p. p. p.	61, 68, 36, 44, 12, 58, 64,	Nov Sep Dec Nov Dec Jun	74 75 74 73 73 74
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØPHF, WAØUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN) W3CIX	p. p. p. p. p. p.	61, 68, 36, 44, 12, 58, 64, 58,	Nov Sep Dec Nov Dec Jun Mar	74 74 75 74 73 73 74 73
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater K⊘PHF, WA⊘UZO Test set for Motorola radios K⊘BKD Short circuit Added note (letter) Timer, simple (HN) W3CIX Tone-burst generator (HN) K4COF	p. p.osp. p.p.p. p.	61, 68, 36, 44, 12, 58, 64, 58,	Nov Sep Dec Nov Dec Jun Mar Mar	74 74 75 74 73 73 74 73 73 73
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØPHF, WAØUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN) W3CIX Tone-burst generator (HN) K4COF Tone-burst keyer for fm repeaters W86PG	p. p. p. p. p. p. p. p. p.	61, 68, 36, 44, 12, 58, 64, 58, 58,	Nov Sep Dec Nov Dec Jun Mar Mar	74 74 75 74 73 73 73 73 73 73
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØHF, WAØUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN) W3CIX Tone-burst generator (HN) K4COF Tone-burst keyer for fm repeaters W8GRG Tone encoder and secondary frequ	p. p. p. p. p. p. p.	61, 68, 36, 44, 12, 58, 64, 58, 58, 58, 20,	Nov Dec Nov Dec Jun Mar Jan	74 74 75 74 73 73 73 73 73 73 73
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØHF, WAØUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN) W3CIX Tone-burst generator (HN) K4COF Tone-burst keyer for fm repeaters W8GRG Tone encoder and secondary frequ oscillator (HN) K8AUH	p. p. p. p. p. p. p. p. p. p.	61, 68, 36, 44, 12, 58, 64, 58, 58, 58, 36, cy 66,	Nov Sep Dec Nov Dec Jun Mar Jan Jun	74 74 75 74 73 73 73 73 73 73 73
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØHF, WAØUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN) W3CIX Tone-burst generator (HN) K4COF Tone-burst keyer for fm repeaters W8GRG Tone encoder and secondary frequ oscillator (HN) K8AUH Tone encoder, universal for vhf fm	p pop p p p p p p p p p p p	61, 68, 36, 44, 12, 58, 64, 58, 58, 36, cy 66,	Nov Sep Dec Nov Dec Jun Mar Mar Jan	74 74 75 74 73 73 73 73 73 72 69
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØPHF, WAQUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN) W3CIX Tone-burst generator (HN) K4COF Tone-burst generator (HN) K4COF Tone encoder and secondary frequ oscillator (HN) K8AUH Tone encoder, universal for vhf fm W6FUB Correction	p p p p p p p p p p p p p p p p p p p	61, 68, 36, 44, 12, 58, 64, 58, 58, 58, 58, 58, 17, 58, 58, 58, 58, 58, 58, 58, 58, 58, 58	Nov Sep Dec Hiov Nov Jun Mar Jan Jun , Jul	74 75 74 73 73 73 73 73 73 73 73 73 73 73 73 73
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØPHF, WAQUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN) W3CIX Tone-burst generator (HN) K4COF Tone-burst generator (HN) K4COF Tone-burst keyer for fm repeaters W8GRG Tone encoder and secondary frequ oscillator (HN) K8AUH Tone encoder, universal for vhf fm W6FUB Correction Touch-tone circuit, mobile K70WR	p pop pop pop pop pop pop pop pop pop p	61, 668, 36, 44, 58, 64, 58, 58, 36, cy 66, 17 58, 58, 58, 58, 58, 58, 58, 58, 58, 58,	Nov Sep Dec Hov Dec Jun Mar Jan Jun Jun Dec Mar	74 74 75 74 73 73 73 73 73 73 73 73 73 72 69 75 75 73
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØPHF, WAØUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN) W3CIX Tone-burst generator (HN) K4COF Tone-burst generator (HN) K4COF Tone-burst keyer for fm repeaters W8GRG Tone encoder and secondary frequ oscillator (HN) K8AUH Tone encoder, universal for vhf fm W6FUB Correction Touch-tone circuit, mobile K7QWR	p p p p p p p p p p p p p p p p p p p	61, 68, 36, 44, 58, 64, 58, 58, 36, 58, 58, 58, 58, 58, 58, 58, 50,	Norv Sep Dec Tilov Dec Jun Mar Jan Jun Jun Dec Mar	74 74 75 74 73 73 73 73 73 73 72 69 75 75 73
<ul> <li>WA2YUD</li> <li>Squelch-audio amplifier for fm receivers</li> <li>WB4WSU</li> <li>Squelch circuits for transistor radi</li> <li>WB4WSU</li> <li>Telephone controller, automatic for your repeater</li> <li>KØPHF, WAØUZO</li> <li>Test set for Motorola radios</li> <li>KØBKD</li> <li>Short circuit</li> <li>Added note (letter)</li> <li>Timer, simple (HN)</li> <li>W3CIX</li> <li>Tone-burst generator (HN)</li> <li>K4COF</li> <li>Tone-burst keyer for fm repeaters</li> <li>W8RG</li> <li>Tone encoder and secondary frequoscillator (HN)</li> <li>K8AUH</li> <li>Tone encoder, universal for vhf fm</li> <li>W6FUB</li> <li>Correction</li> <li>Touch-tone circuit, mobile</li> <li>K7QWR</li> <li>Touch-tone decoder, multi-function</li> <li>KØPHF, WAØUZO</li> <li>Touch-tone decoder, three-digit</li> </ul>	p pop p p p p p p p p p p p p p p	61, 68, 36, 44, 58, 64, 58, 36, 58, 36, 58, 36, 17, 58, 58, 14,	Nov Sep Dec Nov Dec Jun Mar Jan Jun Jun Dec Mar Oct	74 74 75 74 73 73 73 73 73 73 73 73 72 *69 75 75 73 73 73
WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØPHF, WAØUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN) W3CIX Tone-burst generator (HN) K4COF Tone-burst keyer for fm repeaters W8GRG Tone encoder and secondary frequ oscillator (HN) K8AUH Tone encoder, universal for vhf fm W6FUB Correction Touch-tone circuit, mobile K7QWR Touch-tone decoder, multi-function KØPHF, WAØUZO Touch-tone decoder, three-digit W6AYZ Circuit hoard for	p, pop p,	61, 68, 36, 44, 58, 64, 58, 58, 36, 258, 58, 36, 17, 58, 50, 14, 37, 52, 50, 14, 52, 50, 50, 50, 50, 50, 50, 50, 50	Nov Sep Dec Hov Dec Jun Mar Jan Jun Jan Jun Oec Mar Oct Dec	74         74         75         74         75         74         73         74
<ul> <li>WA2YUD</li> <li>Squelch-audio amplifier for fm receivers</li> <li>WB4WSU</li> <li>Squelch circuits for transistor radi</li> <li>WB4WSU</li> <li>Telephone controller, automatic for your repeater</li> <li>KØHF, WAØUZO</li> <li>Test set for Motorola radios</li> <li>KØBKD</li> <li>Short circuit</li> <li>Added note (letter)</li> <li>Timer, simple (HN)</li> <li>W3CIX</li> <li>Tone-burst generator (HN)</li> <li>K4COF</li> <li>Tone-burst keyer for fm repeaters</li> <li>W8RG</li> <li>Tone encoder and secondary frequoscillator (HN)</li> <li>K8AUH</li> <li>Tone encoder, universal for vhf fm</li> <li>W6FUB</li> <li>Correction</li> <li>Touch-tone circuit, mobile</li> <li>K7QWR</li> <li>Touch-tone decoder, multi-function</li> <li>KØHF, WA2UZO</li> <li>Touch-tone decoder, three-digit</li> <li>W6AYZ</li> <li>Circuit board for</li> <li>Touch-tone, hand-held</li> </ul>	p. p	61, 68, 36, 44, 12, 58, 64, 58, 58, 36, 29, 66, 17, 58, 50, 14, 37, 62,	Nov Sep Dec Hov Dec Jun Mar Jan Jan Jun Dec Mar Oct Dec Sep	<b>74 74 75 74 73 73 73 73 73 73 73 73</b>
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WA2YUD Squelch-audio amplifier for fm receivers WB4WSU Squelch circuits for transistor radi WB4WSU Telephone controller, automatic for your repeater KØHFF, WAØUZO Test set for Motorola radios KØBKD Short circuit Added note (letter) Timer, simple (HN) W3CIX Tone-burst generator (HN) K4COF Tone-burst generator (HN) K4COF Tone-burst keyer for fm repeaters W8GRG Tone encoder and secondary frequ oscillator (HN) K8AUH Tone encoder, universal for vhf fm W6FUB Correction Touch-tone decoder, multi-function KØPHF, WAØUZO Touch-tone decoder, three-digit W6AVZ Circuit board for Touch-tone, hand-held K7YAM Touch-tone handset, converting sli K2YAH Transceiver for two-meter fm, com	p pop p pop p p p p p p p p p p p p p p	<b>61.</b> <b>68.</b> <b>36.</b> <b>44.</b> <b>12.</b> <b>58.</b> <b>64.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> <b>58.</b> 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<b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b> <b>17.</b>	Nov Sep Dec Hiov Dec Jun Mar Mar Jan Jun Jun Occ Sep Sep Jun Jan ated	<b>74</b> <b>74</b> <b>74</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> <b>73</b> 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Transmitter, two-meter fm	
W9SEK	p. 6, Apr 72
Tunable receiver modification	
for vhf fm	
WB6VKY	p. 40, Oct 74
Vertical antennas, truth about	%-wavelength
KØDOK	p. 48, May 74
Added note (letter)	p. 54, Jan 75
Weather monitor receiver, retun	e to
two-meter fm (HN)	
W3WTO	p. 56, Jan 75
Whip, 5/8-wave, 144 MHz (HN)	
WE3DDD	p. 70, Apr 73
220 MHz frequency synthesizer	
W6GXN	p. 8, Dec 74
450-MHz preamplifier and conve	erter
WA2GCF	p. 40, Jul 75

## integrated circuits

Amateur uses of the MC1530 IC W2EEY	p.	42,	May	68
Amplifiers, broadband IC W6GXN	D.	36.	Jun	73
Applications, potpourri of IC WIDTY Thoma		8	May	69
Balanced modulator, an integrated	d-ci	rcui	t	
Cross logic circuits	P	. 0,	Sep	70
W3FQJ Counter gating sources	p.	50,	Jun	75
K6KA Counter reset generator (HN)	р.	48,	Nov	70
W3KBM C3L logic circuit	p.	68,	Jan	73
WIDTY Digital counters (letter)	р	. 4,	Mar	75
WIGGN Digital ICa. and L	p.	76,	May	73
W3FQJ	p.	41,	Mar	72
W3FQJ	p.	58,	Apr	72
Correction Digital mixers	р.	66,	Nov	72
WBBIFM Digital multivibrators	p.	42,	Dec	73
W3FQJ Digital applitators and dividers	p.	42,	ากม	72
W3FQJ	р.	62,	Aug	72
K6KA	to-al-	ы. 6,	Feb	72
Digital station accessory, part II K6KA	р.	50,	Mar	72
Digital station accessory, part III K6KA	p.	36,	Apr	72
Electronic counter dials, IC K6KA	ф.	44,	Sep	70
Electronic keyer, cosmos IC WB2DFA	1	<b>5</b> . 6.	Jun	74
Short circuit	p.	62,	Dec	74
W3FQJ	p.	62,	Sep	72
W3FQJ	;p	. 60	, Jul	72
W3KBM	p.	60,	Feb	72
Function generator, IC WIDTY	p.	40,	Aug	71
Function generator, IC K4DHC	p.	22	Jun	74
1C power (HN) W3KBM	p.	68	, Apr	72
IC-regulated power supply for ICs W6GXN	D.	28.	Mar	68
Integrated circuits, part 1 W3F01	г. п	40	lun	71
Integrated circuits, part II	μ.	0,	- Jul	71
Integrated circuits, part III W3FQJ	ч р.	50,	Aug	71

12L logic circuits					-
	, t	).	4,	Nov	75
WEGYN	~		26	lan	74
Logic monitor (HN)	μ.	•	20,	Jan	14
WASSAF	D.		70.	Apr	72
Correction	р.	9	я,	Dec	72
Logic test probe					
VEGRF	p.	5	i3,	Dec	73
Logic test probe (HN)	_				77
Short circuit	p.		. R	Dec	73
Low-cost linear ICs	р.	`	,	Ju	
WA7KRE	p.	1	20,	Oct	69
Modular modulos					
W9SEK	р.	•	53,	Aug	70
Motorola MC1530 IC, amateur use	es t	0	2	May	60
Multi-function integrated circuits	μ.	4	2,	way	00
W3FOJ	D.	2	\$6.	Oct	72
National LM373, using in ssb tran	ISCO	эiv	/er		-
W5BAA	р.	3	2,	Nov	73
Operational amplifiers			~		~~
WB2EGZ	р		ь,	Nov	69
W3FOI	n	F	<b>.</b> 4	Sen	71
Phase-locked loops, IC, experimen	ts	wi	th	ocp	
W3FQJ	р.	5	58,	Oct	71
Plessey SL600-series ICs, how to	use			<b>.</b> .	
G8FNT	р.	2	26,	Feb	73
WENIE	n	7	1	Αμσ	70
Seven-segment readouts, multiple:	xed	'	-,	1146	10
W5NPD	P		37	, Jul	75
Ssb detector, IC (HN)			_	_	
K40DS	р.	6	7.	Dec	72
Seb equipment using TTL ICs is	p.		Ζ,	Apr	13
G4ADJ	n.	1	8.	Nov	75
Surplus ICs (HN)	<b>,</b>	-	-,		
W4AYV	р		68,	, Jul	70
Sync generator, IC, for ATV					
WØKGI	р	•	34,	Jul	75
G3ZVC	n	3	4	Aug	74
Circuit change (letter)	р. D.	6	2	Sen	75
Using ICs in a nbfm system					
W6AJF	p.	3	30,	Oct	68
Using ICs with single-polarity					
worsupplies	<b>n</b>	2	5	Sen	69
Using integrated circuits (HN)	μ.	5	Ξ,	σeμ	05
Wakxi	р.	6	э,	May	69
Voltage regulators, IC					
W/FLC Voltage.regulator (Ca. adjustabl)	p.	2	22,	Oct	70
WR9KEY	n	2	6	Aur	75
Voltage-regulator ICs. three-termin	nal	5	σ,	NUB	, ,
WB5EMI	р.	2	6,	Dec	73
Added note (letter)	p.	7	3,	Sep	74
Vtvm, convert to an IC voltmeter			~	<b>D</b>	74
NOVUL	p.	4	2,	Dec	74

### keying and control

Break-in circuit, CW				
W8SYK	p.	40,	Jan	72
Break-in control system, IC (HN)				
W9ZTK	p.	68,	Sep	70
Bug, solid-state				
Ř2FV	р.	50,	Jun	73
Carrier operated relay				
KØPHF, WAØUZO	p.	58,	Nov	72
Cmos keying circuits (HN)				
WB2DFA	р.	57,	Jan	75
Contest kever (HN)	•			
K2UBC	р.	79,	Apr	70
CW reception, enhancing through	a			
simulated-stereo technique				
WAIMKP	р.	61,	Oct	74

communications				- 4
Leward, WB2EAX Electronic hand keyer	p.	54,	Apr	74
K5TCK Electronic keyer, cosmos IC	р.	36,	תער י	71
WBZDFA Short circuit	p.	62,	Dec	74
VE7BFK Electronic kover potes (HN)	p.	32,	Nov	69
ZLIBN Electronic kever package, compac	p.	74,	Dec	71
W4ATE Electronic keyer with random-acce	p. ess	50, mer	Nov nory	73
WB9FHC	F	o. 6,	Oct	73
Corrections (letter)	p.	58,	Dec	74
	р.	57,	Jun	75
Increased flexibility (HN) Electronic keyer, 8043 IC WGGXN	p.	62,	Mar	75
Electronic keyers, simple IC WA5TRS	ь.	. 8.	Mar	73
Grid-block keying, simple (HN) WA4DHU	р.	78.	Apr	70
Key and vox clicks (HN) K6KA	, р.	74,	Aug	72
Keyboard electronic keyer, the co W6CAB	de p.	mill 38,	Nov	74
Keying, paddle, Siamese WA5KPG	р.	45,	Jan	75
Keying the Heath HG-10B vfo (HN K4BRR	) p.	67,	Sep	70
Latch circuit, dc WØLPQ	p.	42,	Aug	75
Memo-key	р.	58,	Dec	75
Memory accessory, programmable	p.	58,	Jun	12
WA9LUD	p.	24,	Aug	75
K6RIL Morro Constator Keybeard	р.	46,	Feb	69
W7CUU Morse sounder, radio controlled (h	р. чых	36,	Apr	75
K6QEQ Oscillators electronic kever	р.	66,	Oct	71
WA6JNJ Paddle, electronic kever (HN)	р.	44,	Jun	70
KL7EVD Paddle, homebrew keyer	p.	68,	Sep	72
W3NK Push-to-talk for Styleline telephone	p. es	43,	May	69
W1DRP Relay activator (HN)	p.	18,	Dec	71
K6KA Relays, surplus (HN)	р.	62,	Sep	71
W2OLU Relay, transistor replaces (HN)	p.	- 70,	Jul	70
W3NK Relays, undervoltage (HN)	р.	12,	Jan	70
Remote keying your transmitter (H	р. IN)	04, 74	Mar	/1
Reset timer, automatic	р. Б	74, 54	Oct	7.1
Sequential switching (HN) W50SF	р. р.	63.	Oct	72
Solenoid rotary switches W2EEY	р.	36.	Apr	68
Station control center W7OE	р.	26,	Apr	68
Step-start circuit, high-voltage (HN W6VFR	l) p.	64,	Sep	71
Suppression networks, arc (HN) WA5EKA	p.	70,	Jul	73
Time base, calibrated electronic ke WIPLJ	p.	r 39,	Aug	75
ransistor switching for electronic keyers (HN) waopo		66	lu-	74
mayau	μ.	00,	JUN	/4

CW regenerator for interference-free

Transmitter switching, solid-state W2EEY	p. 44, Jun 68
further automation for	
W6PRO	p. 26, Mar 70
Vox and mox systems for ssb	
Belt	p. 24, Oct 68
Vox, IC	
W2EEY	p. 50, Mar 69
Vox keying (HN)	•
VE7IG	p. 83. Dec 69
Vox. versatile	,
W9KIT	p. 50. Jul 71
Short circuit	p. 96, Dec 71

# measurements and test equipment

Ac current monitor (letter)				
WB5MAP	р.	61,	Mar	75
Ac power-line monitor W2OLU	р.	46,	Aug	71
AFSK generator, crystal-controlled K7BVT	р	. 13	, Jul	72
AFSK generator, phase-locked loop K7ZOF	) р.	27.	Mar	73
Amateur frequency measurements K6KA	, D	53.	Oct	68
A-m modulation monitor, vhf (HN)	р,	67	fut	71
Antenna gain, measuring	٣	,	,	
K6JYO Antenna matcher	р	. 26,	, Jul	69
W4SD	p.	24,	Jun	71
Antenna and transmission line				
W40Q	p.	36,	May	74
Beta master, the KRERV	n.	18.	Aug	68
Bridge for antenna measurements	P.	imnl	AUB P	00
W2CTK	, J n	34.	Sen	70
Bridge noise for impedance meas	р. 5118	ome	nts	
VAIGIM	501	62	lan	73
Added notes in 66 May 74:	μ.	60	Mar	75
Bridge, rf noise	μ.	00,	War	15
WB2EGZ	p.	18,	Dec	70
K6KA	p.	41,	Nov	68
Calibrator, plug-in IC K6KA	D.	22.	Mar	69
Capacitance meter, digital	". "	20	Feb	74
Capacitance meter, direct-reading	р. _	16	A	70
Capacitance meter, direct-reading	μ.	40,	Apr	70
W6MUR	р.	48,	Aug	72
Capacitance meter, direct-reading	p.	64,	mar	74
WA5SNZ	p.	32,	Apr	75
Added note	p.	31,	Uct	15
Capacitance meter, direct reading	, fo	)r		
electrolytics W9DJZ	D.	14.	Oct	71
Coaxial cable, checking (letter)				
W2OLU	р.	68,	May	71
Coaxial-line loss, measuring with a reflectometer	a			
W2VCI	p.	50,	Мау	72
Converter, mosfet, for receiver				
instrumentation WA9ZMT	р.	62,	Jan	71
Counter, compact frequency	•			70
K4EEU Short circuit	р а	. 16, 72.	, Jul Dec	70
Counter, digital frequency	۲.	,		
K4EEU Counter gating sources	F	o. 8,	Dec	68
K6KA	р.	48,	Nov	70

Counter readouts, switching (HN) K6KA	p. 66, Jun 71
Counter reset generator (HN) W3KBM	p. 68. Jan 73
Counters: a solution to the reado	ut problem
CRT intensifier for RTTY	n 18 Jul 71
Crystal checker	p. 10, 501 77
Crystal test oscillator and signal	p. 40, reb 74
K4EEU	p. 46, Mar 73
WA4WDK	ers (HN) p. 64, Sep 71
W4YM	p. 42, Jan 69
Curve master, the K8ERV	p. 40, Mar 68
Decade standards, economical (H W4ATE	(N) p. 66, Jun 71
WIGGN	p. 76, May 73
Digital readout station accessory, K6KA	p. 6, Feb 72
Digital station accessory, part II K6KA	p. 50, Mar 72
Digital station accessory, part III K6KA	p. 36, Apr 72
Dipper without plug-in coils W6BLZ	p. 64, May 68
Dummy load and rf wattmeter, lo W2OLU	p. 56, Apr 70
Dummy load low-power vhf WB9DNI	p. 40, Sep 73
Dummy loads, experimental W8YFB	p. 36, Sep 68
Dynamic transistor tester (HN) VE7ABK	p. 65, Oct 71
Electrolytic capacitors, measurem W2NA	p. 70, Feb 71
Fm deviation measurement (lette K5ZBA	r) p. 68. May 71
Fm deviation measurements W3FOJ	p. 52. Feb 72
Fm frequency meter, two-meter W4.IAZ	n. 40. Jan 71
Short circuit	p. 72, Apr 71
K6KA Frequency calibrator general cov	p. 62, Aug 74
W5UQS Frequency calibrator, how to desi	p. 28, Dec 71
W3AEX Frequency measurement of received	p. 54, Jul 71
signals W4AAD	n. 38. Oct 73
Frequency meter, crystal controll	ed (HN)
Frequency scaler, divide-by-ten	n 26 Aug 70
Short circuit	p. 72, Apr 71
W6PBC	p. 41, Sep 72
Added comments (letter)	p. 64, Nov 73
W6PBC	p. 30, Oct 73
Frequency scaler, uht (11C90) WB9KEY	p. 50, Dec 75
Frequency scaler, 500-MHz W6URH	p. 32, Jun 75
Frequency scalers, 1200-MHz WB9KEY	p. 38, Feb 75
Frequency-shift meter, RTTY VK3ZNV	p. 33, Jun 70
Frequency standard (HN) WA7JIK	p. 69, Sep 72
Frequency standard, universal K4EEU	p. 40, Feb 74
Short circuit	p. 72, May 74

Frequency synthesizer, high-frequency		
K2BLA p. 10	5, Oct	72
Function generator, IC W1DTY p. 40	, Aug	71
Function generator, IC K4DHC	2 Jun	74
Gdo, new use for		، ، دە
Grid current measurement in	, Dec	00
grounded-grid amplifiers W6SAI p. 64	. Aug	68
Grid-dip oscillator, solid-state conversion	i of	70
Harmonic generator (HN)	, Jun	, o
W5GDQ p. 76 I-f alignment generator 455-kHz	5, Oct	70
WA5SNZ p. 50	), Feb	74
K4DHC p. 10	, Sep	73
W6KZK p. 67	, Feb	70
Impedance bridge, low-cost RX W8YFB p. 6	. Mav	73
Impedance bridge, simple	Apr	69
Impedance, measuring with swr bridge	, Apr	00
WB4KSS p. 46 Impulse generator, pulse snap diode	, May	75
Siegal, Turner p. 29	), Oct	<b>7</b> 2
VE3GFN p. 2	8, Jul	68
Intermodulation-distortion measurement on ssb transmitters	5	
W6VFR p. 34	, Sep	74
WA8VFK p. 66	, Jan	74
Current monitor mod (letter) p. 61 Logic monitor (HN)	, Mar	75
WA5SAF p. 70	, Apr	72
Logic test probe	, Dec	72
Logic test probe (HN)	, Dec	73
Short circuit p. 58	, Dec	73
W7FS p. 77	, Sep	68
Meter interface, high-impedance Laughlin p. 20	). Jan	74
Meters, testing unknown (HN)	lan '	7 1
Milliammeters, how to use	, Jan	, . 
Mini-spotter frequency checker	, Sep	/5
W70E p. 48 Monitorscope, miniature	Мау	68
WA3FIY p. 34 Monitorscope PTTY	, Mar	69
W3CIX p. 36	, Aug	72
W3KBM p. 6	8, Jul (	69
Multitester (HN) W1DTY p. 63,	May	71
Noise bridge, antenna (HN) K8FFG p. 71	Mav	74
Noise-figure measurements for vhf	lum '	70
Noise figure, vhf, estimating	, Jun .	/ Z
WA9HUV p. 42 Noise generator, 1296-MHz	, Jun .	/5
W3BSV p. 46 Noise generators, using (HN)	, Aug	73
K2ZSQ p. 79 Oscillator, audio	Aug (	58
W6GXN p. 50	, Feb 🛛	73
WGIEL p. 16	, Apr	72
Added notes p. 90 Oscillator, two-tone, for ssb testing	, Dec 1	72
W6GXN p. 11 Oscilloscope calibrator (HN)	, Apr	72
K4EEU p. 6	9, Jul (	69

Oscilloscope, putting it to work	_	61	500	60
Oscilloscope, troubleshooting am	p. 1ate	64, eur	Sep	69
gear with Allen	р.	52.	Aug	69
Oscilloscope voltage calibrator W6PBC	р. П	54	A	72
Panoramic reception, simple	p.	11	Oct	60
Peak envelope power, how to mea	sur sur	е е	Nei	- 00
Phase meter, rf	p.	32,	NOV	74
VE2AYU, Korth Power meter, rf	p.	28,	Apr	73
K8EEG Precision capacitor	p.	26,	Oct	73
W4BRS Pre-scaler ybf (HN)	р.	61,	Mar	68
W6MGI	p.	57,	Feb	73
W5JJ	p.	61,	Dec	74
Allen	p.	64,	Jun	68
Reflectometers K1YZW	D.	65.	Dec	69
Regenerative detectors and a wide	eba	nd a	mpli Mar	fier 70
Repairs, thinking your way throu	gh	БО БО	Fab	71
Resistance standard, simple (HN)	р.	56,	reb	71
Resistor decades, versatile	p.	65,	Mar	/1
W4ATE Rf current probe (HN)	p	. 66,	Jul	71
W6HPH Rf detector, sensitive	p.	76,	Oct	68
WB9DNI Rf generator clip	p.	38,	Apr	73
W1DTY Rf nower meter, low-level	p.	58,	Mar	68
W5WGF Rf signal generator solid-state	p.	58,	Oct	72
VE5FP	p	42,	Jul	70
WB2MPZ	p.	33,	Oct	71
W72TC	р.	23,	Mar	71
RTTY test generator (HN)	p.	96,	Dec	/1
W3EAG RTTY test generator (HN)	p.	67,	Jan	73
W3EAG RX impedance bridge	P۰	59,	Mar	73
W2CTK RX impedance bridge low-cost	p.	34,	Sep	70
W8YFB Safar suicida cord (HN)	p	6,	Мау	73
K6JYO	р.	64,	Mar	71
W6QJW	p.	34,	Jan	73
Signal generator, tone modulated two and six meters	l fo	or		
WA8OIK Signal generator, wide range	p.	54,	Nov	69
W6GXN Signal injection in ham receivers	p.	18,	Dec	73
Allen	p.	72,	May	68
Allen	р.	52,	Apr	68
Slow-scan tv test generator K4EEU	1	o. 6,	Jul	73
S-meter readings (HN) W1DTY	р.	56,	Jun	68
Spectrum analyzer, four channel W91A		. 6.	Oct	72
Spectrum analyzers, understandin WA5SNZ	ຮຼົ	50.	Jun	74
Ssb, signals, monitoring	р. Б	25	Mar	70
Sweep generator, how to use	μ.	ວວ, ແລ	widr	12
Allen	р.	60,	Apr	70

Sweep response curves for low-f	req	uenc	∶y i-f'	s
Allen	p.	56,	Mar	71
Thomas	D	. 64	. Jul	71
Swr bridge WB2ZSH	О	55	, oct	71
Swr bridge and power meter, int	egr	ated		
W6D0B Swr bridge (HN)	р.	40,	Мау	70
WA5TFK Swr bridge readings (HN)	р.	66,	May	72
W6FPO	p.	63,	Aug	73
WEVSV	ţ	o. 6,	Oct	70
Swr meters, direct reading and e	xpa	inde	d sc	ale
WA4WDK Correction	р.	28,	May	72
Time domain reflectometry experi	p. im/	90, ante	Dec.	12
approach to		snie		
WAØPIA	р.	22,	May	71
W6NBI	n	44	Sen	71
Transformer shorts	μ.	,		
Transistor and diode tester	p	. 30	, Jui	68
ZL2AMJ Transistor curve tracer	р.	65,	Nov	70
WA9LCX	p	. 52	, Jul	73
Short circuit	p.	63,	Apr	74
WA6NIL	Ð	. 48	. Jul	68
Transistor tester for leakage and	ga	in	14.000	<b>C</b> 0
Transmitter tuning unit for the b	p. linc	68, I	way	68
W9NTP Trapezoidal monitor scope	p.	60,	Jun	71
VE3CUS	p.	22,	Dec	69
Allen	ρ.	42,	Oct	68
Allen	p.	62,	Nov	68
Troubleshooting transistor ham g Allen	ear p.	64	, Jul	68
Uhf tuner tester for tv sets (HN)	'n	72	Sen	69
Vacuum tubes, testing high-power	(H	N)	Мал	70
W20LU Vhf pre-scaler, improvements for	ρ.	04,	mar	12
W6PBC	p.	30,	Oct	73
Maddever	аπ р.	74,	Apr	68
Voltmeter, transistor, part II Maddever	~	60	ы	68
Vom/vtvm, added uses for (HN)	μ.			
W7DI Vtvm modification	р.	67,	Jan	73
W6HPH Vive convert to an IC voltmeter	p.	51,	Feb	69
K6VCI	p.	42,	Dec	74
Wavemeter, indicating W6NIF	р.	26,	Dec	70
Short circuit	p.	72,	Apr	71
Weak-signal source, stable, variat	ole-(	outp	ut	<b>→</b> .
Weak-signal source, 144 and 432 l	р. ИН:	ან, z	Sep	/1
K6JC Weak-signal source 432 and 1296	р. Мн	58, 17	Mar	70
K6RIL	p.	20,	Sep	68
WWW receiver, simple regenerative WA5SNZ	э р.	42,	Apr	73
WWV-WWVH, amateur application: W3FO.(	s fo	or 52	lan	70
Zener tester, low-voltage (HN)	μ.			
NJUPJ	p.	72,	Nov	69

### miscellaneous technical

Alarm, wet basement (HN) W2EMF p. 68, Apr 72

Amateur anemometer	
W6GXN	p. 52, Jun 6
Antenna masts, design for pipe	p. 54, Aug 6
W3MR Added design notes (letter)	р. 52, Sep 7 р. 75, May 7
Antennas and capture area K6MIO	p. 42, Nov 6
Bandpass filter design K4KJ	p. 36, Dec 7
Bandpass filters for 50 and 144 I W5KHT	MHz, etched p. 6, Feb 7
Bandpass filters, single-pole W6HPH	р. 51, Sep 69
Basic electronic units W2DXH	p. 18. Oct 6
Batteries, selecting for portable e WBØAIK	o, 40, Aug 7
Broadband amplifier, wide-range W6GXN	p. 40. Apr 74
Bypassing, rf, at uhf WB6BHI	n 50 lan 7
Capacitors, oil-filled (HN)	p. 66, Dec 7
Clock, 24-hour digital	p. 00, Dec 72
Short circuit	p. 51, Apr 70 p. 76, Sep 70
K3SVC	p. 6, Apr 71
for strong-signal performance	ning
Moore Computer-aided circuit analysis	p. 6, Feb 73
KIORV Converting vacuum tube equipme	p. 30, Aug 70 ent to
solid-state	n 20 Aug 69
Converting wavelength to inches	(HN)
WA6SXC Current flow?, which way does	p. 56, Jun 68
W2DXH Digital mixer, introduction	p. 34, Jul 68
WB8IFM Digital readout system, simplified	p. 42, Dec 73
W60IS Double-balanced mixers	p. 42, Mar 74
WIDTY Double-balanced modulator, broad	p. 48, Mar 68 dband
WA6NCT Farth currents (HN)	p. 8, Mar 70
W7OUI Effective radiated power (HN)	p. 80, Apr 70
VE7CB	p. 72, May 73
WSJJ	p. 48, Oct 70
KIORV	p. 34, Mar 73
W3FQJ	p. 61, Nov 72
MHz, etched	14
W5KHT Filters, active for direct-conversion	p. 6, Feb 71 n receivers
W7ZOI Fire extinguishers (letter)	p. 12, Apr 74
W5PGG Fire protection	p. 68, Jul 71
Darr Fire protection (letter)	p. 54, Jan 71
K7QCM	p. 62, Aug 71
W6SAI Short circuit	p. 8, Sep 69
Freon danger (letter)	_ co Mar 70
Frequency multipliers	p. 63, May 72
Frequency multipliers, transistor	p. 0, Aug /1
Frequency synchronization for sc	p. 49, Jun 70 atter-mode
propagation K2OVS	p. 26, Sep 71

Frequency synthesis WA5SKM	p. 4	2,	Dec	69
Frequency synthesizer, high-frequency K2BLA	p. 1	16,	Oct	72
Gamma-matching networks, how W7ITB	tode:	sig 6,	n Mav	73
Glass semiconductors W1EZT	0.	54.	Jul	69
Graphical network solutions W1NCK, W2CTK	р. 2		Dec	69
Gridded tubes, vhf-uhf effects W6UOV	- · ·	8.	Jan	69
Grounding and wiring W1FZT	р. 4	4.	Jun	69
Ground plow	p. 4	A .	May	70
Harmonic output, how to predict	μ. υ.	т, Л	Nov	70
Heatsink problems, how to solve	μ	41) 16	lon	74
Hybrids and couplers, hf	р. ч	,	Jan	74
Short circuit	р п. 7	2.	Dec	70
Impedance-matching systems, de	signir	ıg		
W7CSD Inductors, how to use ferrite and	р.	58,	Jul	73
powdered-iron for		~		
Wegan	p. 1	.»,	Apr	/1
Infrared communications (letter)	р, в.	э,	way	12
K2OAW	р. 6	5,	Jan	72
Mims	p. 6	i4,	Apr	71
Mims	p. 2	8,	Sep	71
W3FQJ	p. 4	0,	Jun	71
W3FQJ	р. !	58,	Jul	71
W3FQJ	p. 5	0,	Aug	71
K6KA	p. 6	з,	Mar	75
W1DTY	p. 1	2,	Dec	70
G3LLL	р. 6	5,	Nov	75
WA3NFW	p. 3	0,	Mar	73
G3LLL	те р. 2	6,	Jun	75
Intermittent voice operation of pe	ower			
W6SAL	p. 2	4.	Jan	71
Isotropic source and practical an	tenna	5		• -
K6FD	p. 32	2,	May	70
W4KAE	p. 2	8,	Nov	70
LED experiments W4KAE	p.	6,	Jun	70
Lighthouse tubes for uhf W6UOV	p. 2	7,	Jun	69
Local-oscillator waveform effects				
Robinson. Smith	p. 4	4,	Jun	74
Lowpass filters for solid-state line	ar am	npli	ifiers	
WAØJYK	p. 3	8,	Mar	74
Short circuit	р. 6	2,	Dec	74
Linetworks, how to design		c	<b>F</b> -1	7.4
W/LR Short circuit	p. 2	ь, 2	Feb Dec	14 74
Snort circuit Lunar-nath nomograph	р, о	۷,	Dec	74
WA6NCT	p. 2	8,	Oct	70
Marine installations, amateur, on	small	bo	oats ∧u~	74
Microprocessors introduction to	p. 4	+, .	Ang	74
WB4HYJ, Rony, Titus	p. 3	2,	Dec	75
Roubal	p, 5	3,	Jun	72
WICrowaves, Introduction WICBY	p. 2	٥,	Jan	72

Mini-mobile	~	50	A	71
Mismatched transmitter loads, aff	ect	of	Aug	
W5JJ Mnemonics	р.	60,	Sep	69
W6NIF More electronic units	р.	69,	Dec	69
W1EZT Multi-function integrated circuits	<b>p</b> .	56,	Nov	68
W3FQJ Networks, transmitter matching	p.	46,	, Oct	72
Neutralizing small-signal amplifie	rs_F	o. 6,	Jan	73
Noise figure, meaning of	р.	40,	Sep	70
K6MIO Operational amplifiers	р.	26,	Mar	69
WB2EGZ Phase detector, harmonic	p	6, 6,	Nov	69
W5TRS Phase-locked loops, IC	р.	40,	Aug	74
W3FQJ Phase-locked loops, IC, experimen	p. ts	54, with	Sep	71
W3FQJ Phase shift networks, design crite	р. ria	58, for	Oct	71
G3NRW Pi and pi-1 networks	р.	34,	Jun	70
W6SAI Pì network design	ρ.	36,	Nov	68
W6FFC Bi network inductors (letter)	p	. 6,	Sep	72
W7IV Pi. potworka, posice tupod	ρ.	78,	Dec	72
W2EGH	р.	42,	Oct	71
WB8LQK	r F	s. 8,	Oct	74
W1DAX	p.	30,	Aug	72
Power supplies, survey of solid-sta W6GXN	ate p.	25,	Feb	70
Power, voltage and impedance no W2TQK	та, р.	grap 32,	h Apr	71
Printed-circuit boards, photofabric	atio	on of	Sen	71
Programmable calculator simplifie	es "	,	000	
W3DVO	p.	70,	May	74
W3DVO	p.	40,	Mar	75
Proportional temperature control ovens	for	crys	stal	
VESFP Pulse-duration modulation	p.	44,	Jan	70
W3FQJ Q factor, understanding	p.	65,	Nov	72
W5JJ QRP operation	p.	16,	Dec	74
W70E Radiation hazard, rf	p.	36,	Dec	68
W1DTY Correction	p n.	. 4, 59.	Sep Dec	75 75
Radio communications links W1EZT	р. р.	44.	Oct	69
Radio observatory, vhf Ham	n	44	hul	74
Radio-frequency interference	р. п	, 	Mar	72
Radiotelegraph translator and tran	μ. 15CI	riber	Nov	73
Eliminating the matrix	μ	,	NUV	71
Ramp generators	р.	Б <b>О</b> ,	мау	12
woGXN Rating tubes for linear amplifier	p.	56,	Dec	68
W6UOV, W6SAI	р.	50,	Mar	71
W6NIF	p.	51,	Sep	70
Resistor performance at high free K1ORV	p.	ncie: 36,	s Oct	71
Resistors frequency sensitive (HN	• •			

Resistors, frequency sensitive (let	iter)	
RF amplifier, wideband	р. 68, Jul /1	
WB4KSS Rf power-detecting devices	p. 58, Apr 75	5
K6JYO Rf power transistors, how to use	p. 28, Jun 70	
WA7KRE Safety in the ham shack	p. 8, Jan 70	
Darr, James Satellite communications first st	p. 44, Mar 69	•
K1MTA	p. 52, Nov 72	
Satellite signal polarization	p. /3, Apr /3	
KH6IJ Signal detection and communicati	p. 6, Dec 72 ion	
in the presence of white noise WB6IOM	p. 16, Feb 69	
Silver/silicone grease (HN)	n 63 May 71	
Single-tuned interstage networks,	p. 05, Way /1	
K6ZGQ	p. 59, Oct 68	
Smith chart, how to use WIDTY	p. 16, Nov 70	
Correction Solar activity, aspects of	p. 76, Dec 71	
K3CHP Solar energy	p. 21, Jun 68	
W3FQJ Spageb clippore of performance	p. 54, Jul 74	
G6XN	p. 26, Nov 72	
Square roots, finding (HN) K9DHD	p. 67, Sep 73	
Increased accuracy (letter) Standing-wave ratios, importance	p. 55, Mar 74 of	
W2HB Correction (letter)	p. 26, Jul 73	
Stress analysis of antenna system	ns - 03 Oct 71	
W2r2J Tetrodes, external-anode	p. 23, 001 /1	
W6SAI Thermoelectric power supplies	p. 23, Jun 69	
K1AJE Thermometer, electronic	p. 48, Sep 68	
VK3ZNV	p. 30, Apr 70	
W6HPH	p. 79, Aug 68	
WA7KRE	p. 54, Oct 70	
W3WLX	p. 26, Sep 75	
Toroids, calculating inductance of WB9FHC	f p. 50, Feb 72	
Toroids, plug-in (HN) K8EEG	p. 60. Jan 72	
Transistor amplifiers, tabulated		
W5JJ Trig functions on a necket coloulat	p. 30, Mar 71	
W9ZTK	p. 60, Nov 75	
K2ZSQ	p. 38, Jan 69	
TV sweep tubes in linear service, full-blast operation of		
W6SAI, W6OUV Vacuum-tube amplifiers, tabulated	p.9,Apr68 d	
characteristics of W5JJ	p. 30, Mar 71	
Warning lights, increasing reliabil W3NK	lity of D 40 Feb 70	
Wind direction indicator, digital	p. 40, reu /V	
Wind loading on towers and anten	р. 14, Sep 68 na	
structures, how to calculate K4KJ	p. 16, Aug 74	
Added note Y parameters, using in rf amplifier	p. 56, Jul 75 r design	
WAØTCU	p. 46, Jul 72	

## operating

Beam antenna headings				
W6FFC	p.	64,	Apr	71
Code practice stations (letter)				
WB4LXJ	р.	75,	Dec	72
Code practice — the rf way				
WA4NED	p.	65,	Aug	68
Code practice (HN)				
W2OUX	р.	74,	May	73
Computers and ham radio				
W5TOM	ρ.	60,	Mar	69
CW monitor				
W2EEY	p.	46,	Aug	69
CW monitor and code-practice osc	illa	tor		
KGRIL	р.	46,	Apr	68
CW monitor, simple				
WA9OHR	p.	65,	Jan	71
CW transceiver operation with				
transmit-receive offset				
WIDAX	p.	56,	Sep	70
DXCC check list, simple				
W2CNQ	p.	55,	Jun	73
Fluorescent light, portable (HN)			_	
K8BYO	p.	62,	Oct	73
Great-circle charts (HN)		~~	<u>.</u>	
KOKA	р.	62,	Oct	73
		50		<b>c</b> 0
Identification times (UN)	ρ.	58,	Mug	00
KOLION	_	60	Nou	74
Magazines, use your eld	р.	60,	1100	74
Foster	-	50	120	70
Morse code speed standards for	μ.	JZ,	Jan	10
VF27K	-	68	Anr	73
Added note (letter)	р.	68	lan	74
Protective material plastic (HN)	μ.	00,	5011	/ 1
W6BKX	n	58	Dec	70
OSI return statistics on	μ.	50,	0.0	
WREILIH	n	60	Dec	68
Replays, instant (HN)	μ.	,	0.0	00
W6DNS	n.	67.	Feb	70
Sideband location (HN)	P	~.,		
K6KA	p.	62.	Aug	73
Spurious signals (HN)		,		
K6KA	p.	61.	Nov	74
Tuning with ssb gear		•		
WØKD	р.	40,	Oct	70
Zulu time (HN)	•			
КбКА	p.	58,	Mar	73

### oscillators

AFSK oscillator, solid-state				
WA4FGY	p.	28,	Oct	68
Audio oscillator, NE566 1C	~	36	lan	75
Blocking oscillators	р.	50,	Jan	/5
W6GXN	Ð.	45.	Apr	69
Clock oscillator, TTL (HN)			•	
W9ZTK	р.	56,	Dec	73
Crystal oscillator, frequency adjust	stm	ento	of	
W9ZTK	ρ.	42,	Aug	72
Crystal oscillator, high stability	•		-	
W6TNS	p.	36,	Oct	74
Crystal oscillator, miniature				
W6DOR	p.	68,	Dec	68
Crystal oscillators				
W6GXN	p.	33,	Jul	69
Crystal oscillators, stable				
DJ2LR	р.	34,	Jun	75
Correction	ρ.	67,	Sep	75
Crystal switching (HN)				
KELZM	ρ.	70,	Mar	69
Crystal test oscillator and signal	•			
Sellerator	_	46	14.0.0	72
	р.	40,	mar	13
Crystals, overtone (HN)				70
G8ABK	р.	72,	Aug	72

,

Hex inverter vxo circuit W2LTJ	<b>D</b> .	50.	Apr	75
Local oscillator, phase locked VESFP		6.	Mar	7)
Monitoring oscillator W2110		36	Dec	72
Multiple band master-frequency os	scil	lato,	Nov	75
Multivibrator, crystal-controlled	μ.	50,		70
Oscillator, audio, IC	ч _	. 65	, Jui	71
Oscillator, electronic keyer	р. 	50,	reo	73
Oscillator, Franklin (HN)	р.	44,	Jun	70
WSJJ Oscillator, frequency measuring	р.	61,	јап	72
Added notes	р. р.	16, 90,	Apr Dec	72 72
Oscillator, gated (HN) WB9KEY	р	. 59,	, Jul	75
Oscillator-monitor, audio WAIJSM	р.	48,	Sep	70
Oscillator, phase-locked VE5FP	р	. 6,	Mar	71
Oscillator, two-tone, for ssb testing W6GXN	g p.	11,	Apr	72
Oscillators (HN) W1DTY	р.	68,	Nov	69
Oscillators, cure for cranky (HN) W8YFB	р,	55,	Dec	70
Oscillators, repairing Allen	р.	69.	Mar	70
Oscillators, resistance-capacitance W6GXN	י ס	. 18.	Jut	72
Oscillators, ssb Belt	n.	26.	Jun	68
Overtone oscillator (HN) W5HOS	n.	77.	Oct	68
Quadrature-phased local oscillator	(le	tter)	Sen	75
Quartz crystals (letter)	р. Б	74	Dec	72
TTL crystal oscillators (HN)	р. 	, <del>,</del>	Aur	75
Vco, crystal-controlled	р. _	бU, БО	Aug	75 60
Vfo buffer amplifier (HN)	р.	58,	Uct	71
W3QBO Vfo, digital readout	р	. 60,	, 301	71
VIO for solid-state transmitters	р.	14,	Jan	73
W3QBO Vfo, high stability	р.	36,	Aug	70
Vfo, high-stability, vhf	р.	14,	Mar	59
Vfo, multiband fet	р.	27,	Jan	72
K8EEG Vfg, stable	p	. 39,	- Jul	12
K4BGF Vfo, stable transistor	P	. 8,	Dec	71
WIDIY Short circuit	р. р.	14, 34,	Jun Aug	68 68
Vfo transistors (HN) W100P	p.	74,	Nov	69
Vxo design, practical K6BIJ	p.	22,	Aug	70
455-kHz bfo, transistorized W6BLZ, K5GXR	p	. 12,	Jul	68

### power supplies

Ac current monitor (letter)				
WB5MAP	р.	61,	Mar	75
Ac power supply, regulated, for me	obi	e		
fm equipment				
WASTMP	р.	28,	Jun	73
Arc suppression networks (HN)				
WA5EKA	р.	70,	Jut	73

Batteries, selecting for portable e	quipment
Battery drain, auxiliary, guard for	p.40,Aug./3 (HN)
WIDTY	p. 74, Oct 74
Battery power	55 Aug 74
Charger, fet-controlled, for nicad	batteries
WAØJYK Current limiting (HN)	p. 46, Aug 75
WØLPQ	p. 70, Dec 72
Current limiting (letter) K5MKO	p. 66, Oct 73
Dc-dc converter, low-power W5MLY	p. 54, Mar 75
Diodes for power supplies, choos W6BLZ	ing p. 38, Jul 68
Diode surge protection (HN)	n 65 Mar 72
Added note	p. 77, Aug 72
W100P	p. 71. Apr 69
Short circuit	p. 80, Aug 69
Dual-voltage power supply (HN) W5JJ	p. 68, Nov 71
Filament transformers, miniature	p. 66. Sep 74
High-power trouble shooting	p 52 Aug 68
IC power (HN)	p. 52, Aug 08
W3KBM IC regulated power supply	p. 68, Apr 72
W2FBW IC regulated power supply	p. 50, Nov 70
W9SEK IC regulated power supply for ICs	p. 51, Dec 70
W6GXN Shart circuit	p. 28, Mar 68 p. 80, May 68
Klystrons, reflex power for (HN) W6BPK	p. 71, Jul 73
Line transient protection (HN) W1DTY	n. 75. Jul 68
Line-voltage monitor (HN)	p. 66 Jap 74
Current monitor mod (letter)	p. 61, Mar 75
W50ZF	p. 62, Oct 72
WA5EKA	p. 66, Nov 71
Low-voltage supply with short-circ	uit
WB2EGZ	p. 22, Apr 68
Low-voltage supply (HN) WB2EGZ	p. 57. Jun 68
Meter safety (HN)	p 69 Jul 72
Mobile power supplies, troublesho	p. 66, Jul 72 poting
Alien Mobile power supply (HN)	p. 56, Jun 70
WN8DJV	p. 79, Apr 70
W4GEG	p. 69, Jul 70
Motorola Dispatcher, converting t 12 volts	0
мвенхи	p. 26, Jul 72
WA2IKL	p. 8, Apr 70
Pilot-lamp life (HN) W2OLU	p. 71. Jul 73
Polarity inverter, medium current	5 26 Nov 73
Power supplies for single sideban	d
Power-supply hum (HN)	p. 38, FED 69
W8YFB Power supply, improved (HN)	p. 64, May 71
W4ATE Power supply, precision	p. 72, Feb 72
W7SK	p. 26, Jul 71
rower supply protection for your circuits	soud-state
W5JJ	p. 36, Jan 70

Precision voltage supply for phase-locked terminal unit (HN)				
WA6TLA Protection for colid state power of	p	60	, Jul	74
W3NK	p. p.	66,	Sep	70
Bailey	р.	34,	Oct	73
Regulated solid-state high-voltage power supply				
W6GXN Short circuit	р. р	40, 69	Jan Anr	75 75
Regulated 5-volt supply (HN) W6UNF	р. р.	67.	Jan	73
SCR-regulated power supplies W4GOC	р. D.	52	Jul	70
Solar energy W3FOJ	D	. 54	. Jul	74
Solar power W3FOJ	р.	52.	Nov	74
Step-start circuit, high-voltage (HN W6VFR	(И . ст	64.	Sep	71
Storage-battery QRP power W3FQJ	р.	64.	Oct	74
Survey of solid-state power suppli- W6GXN	es	25	Feb	70
Short circuit	р.	76,	Sep	70
Thermoelectric power supplies K1AJE	ρ.	48,	Sep	68
Transformers, high-voltage, repair W6N1F	ing p.	66	Mar	69
Transformer shorts W6BLZ	p.	36,	Jul	68
Transformers, miniature (HN) W4ATE	p.	67,	Jul	72
Transients, reducing W5JJ	р.	50,	Jan	73
Vibrator replacement, solid-state ( K8RAY	HN p.	) 70,	Aug	72
Voltage regulators, IC W7FLC	р.	22,	Oct	70
Voltage regulator ICs, adjustable WB9KEY	р.	36,	Aug	75
Voltage-regulator ICs, three-termin WB5EMI	al D.	26.	Dec	73
Added note (letter)	p.	73,	Sep	74
W3FQJ Zepar diadas (HNI)	p.	50,	Jan	75
K3DPJ	<b>p</b> .	79,	Aug	68

### propagation

Artificial radio aurora, scattering				
characteristics of	-	10	Nou	74
VIBONAF Febace lang delay	р.	10,	NOV	74
MIDEKAD	_	<b>G</b> 1	Mou	60
Innecharia E lavor	ρ.	01,	way	69
WR6KAP	<b>n</b>	58	Aug	69
lonospheric science short history	of	001		••
WB6KAP	D.	58.	Jun	69
Long-distance high frequency com	m	inica	ations	;
WB6KAP	р	. 80	, Jul	68
Maximum usable frequency, predi	ctir	٦g		
WB6KAP	p.	70,	Sep	68
Quiet sun, the				
WB6KAP	р.	76,	Dec	68
Scatter-mode propagation, frequer	ncy			
synchronization for				
K2OVS	ρ.	26,	Sep	71
Solar cycle 20, vhter's view of				
WA5IYX	р.	46,	Dec	74
Sunspot numbers				
WB6KAP	р	. 63	Jul	69
Sunspot numbers, smoothed		70		~ ~
WB6KAP	p.	72,	Nov	68
Sunspots and solar activity	_	60	1	~~
WBONAP	р.	<i>ю0</i> ,	Jan	69
woekap		15	0	60
WDONAF	р.	08,	oct	09

6-meter sporadic-E openings,	predictir	g		
WA9RAQ	р.	38.	Oct	72
Added note (letter)	р.	69,	Jan	74

## receivers and converters

#### general

Antenna impedance transformer f	or			
receivers (HN) Wente		70	lan	70
Antenna tuner, miniature receiver	(H	N)	Mar	60
Anti-QRM methods	μ. ~	72, E0	May	71
Attenuation pads, receiving (letter	р. )	50,	мау	71
Audio agc amplifier	p.	69,	Jan	74
Audio agc principles and practice	p.	32,	Uec	73
Audio amplifier and squelch circuit	p. it	28,	Jun	71
W6AJF Audio filter for CW, tunable	p.	36,	Aug	68
Audio filter-frequency translator fo	p. pr C	34, CW	Aug	70
reception W2EEY	p.	24,	Jun	70
Audio filter mod (HN) K6HIU	p.	60,	Jan	72
Audio filter, simple W4NVK	p.	44,	Oct	70
Audio filters, CW (letter) 6Y5SR	р.	56,	Jun	75
Audio-filters, inexpensive W8YFB	p.	24,	Aug	72
Audio filter, tunable peak-notch W2EEY	р.	22,	Mar	70
Audio filter, variable bandpass W3AEX	р.	36,	Apr	70
Audio module, complete K4DHC	р.	18,	Jun	73
Batteries, how to select for portab equipment	le			
WAØAIK Bfo multiplexer for a multimode de	p. ete	40, ctor	Aug	73
WA3YGJ Calibrator crystals (HN)	p.	52,	Oct	75
K6KA Calibrator, plug-in frequency	p.	66,	Nov	71
K6KA Calibrator, simple frequency-divide	p. er	22,	Mar	69
using mos lCs W6GXN	p.	30,	Aug	69
Communications receivers, design Moore	ide p.	eas f 12,	or Jun	74
Communications receivers, design for strong-signal performance	ing			
Moore Converting a vacuum-tube received	р rto	. 6,	Feb	73
solid-state W100P	n.	26.	Feb	69
Counter dials, electronic	р. п	44	Sen	70
CW filter, adding (HN)	р. -	, 	Sep	70
CW monitor, simple	μ.	оо, ст	Jep	73
CW processor for communications	p. re	ceivi	Jan ers	71
WONKW CW reception, enhancing through a	р. а	17,	Oct	71
simulated-stereo technique WA1MKP	p.	61,	Oct	74
CW reception, noise reduction for W2ELV	р.	52,	Sep	73
CW regenerator for interference-fre communications	e			
Leward, Libenschek	p.	54,	Apr	74

CW selectivity with crystal bandpassing				
W2EEY CW transceiver operation with tra	р. nsr	nit-r	eceiv	69 e
W1DAX Detector, reciprocating	p.	56,	Sep	70
WISNN	p.	32,	Mar	72
Added notes p. 54, Mar /4; Detector, superregenerative, optin Ring	p. niz	76, ing 32	May	75
Detectors, ssb	_			
Diversity receiving system	р. –	12	Dec	58
Filter alignment	μ.	12,	Dec	71
Filter, vari-Q	р.	61,	Aug	75
WISNN Frequency calibrator, how to desig	p. gn	62,	Sep	73
W3AEX Frequency calibrator, receiver	Þ	. 54	, Jul	71
W5UQS Frequency measurement of receiv	p. ed	28,	Dec	71
signals W4AAD	p.	38.	Oct	73
Frequency spotter, general covera	ge	36	Nov	70
Frequency standard (HN)	μ.	50,		70
Frequency standard, universal	p.	69,	Sep	12
K4EEU Short circuit	р. р.	40, 72,	Feb May	74 74
Hang agc circuit for ssb and CW WIFR!	'n	50	Sen	72
Headphone cords (HN) W20LU	р. п	62	Nov	75
I-f cathode jack	μ.	02,	6	
I-f system, multimode	p.	28,	Sep	68
WA21KL Image suppression (HN)	p.	39,	Sep	71
W6NIF Intelligibility of communications r	p. ece	68, iver	Dec s,	72
WA5RAQ	p.	53,	Aug	70
Interference, electric fence K6KA	D	. 68	. Jul	72
Interference, hi-fi (HN) K6KA	'n	63	Mar	75
Interference, rf	р.	10		75
Interference, rf	р.	12,	Dec	70
WA3NFW Interference, rf, its cause and cure	p. e	30,	Mar	73
G3LLL Local oscillator, phase-locked	p.	26,	Jun	75
VE5FP Local-oscillator waveform effects	p	. 6,	Mar	71
on spurious mixer responses Robinson, Smith	р.	44,	Jun	74
Mixer, crystal W2LTJ	р.	38,	Nov	75
Noise blanker K4DHC	р,	38,	Feb	73
Noise blanker, hot-carrier diode W4KAE	, р.	16.	Oct	69
Short circuit Noise blanker, IC	p.	76,	Sep	70
W2EEY Short_circuit	р. Р	52, 79	May	69 70
Noise figure, the real meaning of	р. р	26	Mar	60
Panoramic reception, simple W2FFY	р. r	11	0-+	69
Phase-shift networks, design criter	ia Tia	14, 24		70
Product detector, hot-carrier diode	p.	34,	Jun	70
VE3GEN Radio-direction finder	p.	12.	Oct	69 
W6JTT Radio-frequency interference	р.	38,	Mar	70
WA3NFW	р.	30,	Mar	73

Radiotelegraph translator and translator	nsc	ribe	r	
W7CUU, K7KFA	ρ	. 8,	Nov	71
Eliminating the matrix				
КНБАР	р.	60,	Мау	12
Receiver impedance matching (Hr	N)	-	•	~~
WØZEN Resoluting RTTV outernatio frague	р.	, 79,	Aug	68
control for	ncy			
W5NPO	-	50	San	71
Reciprocating detector as fm disc	rim	inati	Jeh Jr	/1
WISNN	n	18	Mar	73
Reciprocating-detector converter	Ρ.	10,		/ 5
WISNN	р.	58.	Sep	74
Rf amplifiers for communications	rec	eive	rs	
Moore	p.	42,	Sep	74
Rf amplifier, wideband				
WB4KSS	p.	58,	Apr	75
S-meter readings (HN)		_		
WIDTY	р.	56,	Jun	68
Selectivity, receiver (letter)		~~		
K4ZZV Sensitivity poice figure and dynam	р.	68,	Jan	74
WIDTY	nic r	ran;	Oct	75
S-meters, solid-state		<i>.</i> 0,	001	/0
K6SDX	p.	20,	Mar	75
Spectrum analyzer, four channel	•			
W9IA	F	b. 6,	Oct	72
Squelch, audio-actuated		~~		-
K4MUG Sab aizaala maaitaalaz	p.	52,	Apr	12
WEVED	-	36	Mar	72
Superregenerative detector, ontin	uzi	190, ng	wai	12
Ring	<u>n</u> .	32	Jut	72
Superregenerative receiver, impro	ved			
JA1BHG	р.	48,	Dec	70
Threshold-gate/limiter for CW rece	epti	on		
W2ELV	р.	46,	Jan	72
Added notes (letter)				-
WZELV Waak signal recention in CW recei	р.	59, c	May	72
7S6RT	ver	3 44	Nov	71
	μ.	441	1107	· •
high-frequency rece	۶Í۱	/er	'S	

#### e 1 icy I çe

Bandpass filters for receiver prese	elec	tors	E.L	75
W/201	_р.	18,	reo	/0
Bandpass tuning, electronic, in th	eι	Jrake	e R-4	C
Horner	p.	58,	Oct	73
BC-603 tank receiver, updating th	e			
WA6IAK	n.	52.	Mav	68
BC-1206 for 7 MHz, converted	<b>P</b> .	,		
W4FIN	p.	30,	Oct	70
Short circuit	Ď.	72.	Apr	71
Collins 75A4 hints (HN)	<b>P</b> = -	,		
W6VFR	n.	68.	Apr	72
Collins 75A.4 modifications (HN)	μ.	,		
W4SD	n	67	lan	71
Communications receiver five bar	ъ.	•,	5411	
KESDY	, u	6	fun	72
Communications receiver for 90	F	J. U,	Jun	12
motors IC				
VESELD			11	71
		h. o	, Jui	/1
communications receiver, micropi	DWE	er		
WB9FHC	p.	30,	Jun	73
Short circuit	p.	58,	Dec	73
Communications receiver, miniatu	rize	ed		
K4DHC	р.	24,	Sep	74
Communications receiver, solid-sta	ate			
ISTDJ	p.	32,	Oct	75
Correction	р.	59,	Dec	75
Companion receiver, all-mode	•			
WISNN	p.	18,	Mar	73
Converter, hf. solid-state				
VE3GEN	~	32	Feh	72
Converter turned your low frames	. <b>р</b> .	J2,	160	12
Ought output	зу	40		
	р.	49,	NOV	74
Direct-conversion receivers				
W3FQJ	р.	59,	Nov	71
Direct-conversion receivers, impro-	ved			
selectivity				
K6BIJ	р.	32,	Apr	72

Direct-conversion receivers,				
simple active filters for		• •	-	
W7201 FSSA weather receiver	p.	12,	Apr	74
W6GXN	p.	36,	May	68
Fet converter, bandswitching, for 40, 20, 15 and 10 (VE3GFN)		p. 6	, Jul	68
postscript	р.	68,	May	69
Fet converter for 10 to 40 meters,	se	conc	1.	
generation	-	20	1	70
VE3GEN Short circuit	p.	28,	Jan	70
Frequency synthesizer for the Ora	p. ke	R.4	5011	/0
W6NBI		6.	Aug	72
Modification (letter)	p.	74,	Sep	74
Gonset converter, solid-state modi	fica	ation	of	
Schuler	p.	58,	Sep	69
Hammarlund HQ215, adding 160-r	ne	ter		
MOCHK		32	ian	72
Heath SB-650 frequency display, L	ısir	יבי, ופ	5411	
with other receivers		.0		
K2BYM	p.	40,	Jun	73
High dynamic range receiver input	st	ages	5	-
DJ2LR	p.	26,	Oct	/5
transceiver adding				
VE3GEN	D.	66.	Feb	71
Monitoring oscillator		,		
W2JIO	p.	36,	Dec	72
Outboard receiver with a transceiv	er	••	~	~~
WIDTY Outboard receiver with the SR 100	p.	12,	Sep	68
Untoolard receiver with the SB-100	,			
K4GMR	р.	68.	Feb	70
Overload response in the Collins 7	SA	-4		
receiver, improving				
W6ZO	ρ.	42,	Apr	70
Short circuit Passing type sch receiver	p.	76,	Sep	70
WAØJYK	D	6.	Aug	73
Short circuit	p.	58,	Dec	73
Added note (letter)	p.	63,	Jun	74
Preamplifier, emitter-tuned, 21 Mh	z	• •		70
WASSNZ Recomplifier law poice high gain t	р.	20,	Apr	12
w2FFY	n.	66	Feb	69
Preselector, general-coverage (HN	) []	,		•••
W5OZF	ρ.	75,	Oct	70
Q5er, solid-state		~ ~		~ •
WOIKP Receiver incremental tuning for th	р.	20,	Aug	69
Swan 350 (HN)	¢			
KIKXA	р	. 64	Jul	71
Receiver, reciprocating detector				
WISNN Correction (latter)	р.	44,	Nov	72
Receiver, versatile solid-state	h.	<i>''</i> ,	Dec	12
W1PLJ	р	. 10,	Jul	70
Receiving RTTY with Heath SB rec	eiv	/ers	(HN)	
K9HVW	р.	64,	Oct	71
Kt amplitiers, selective	<b>n</b>	69	Fab	72
Regenerative detectors and a wide	р. ва	nd,	160	12
amplifier for experimenters				
W8YFB	р.	61,	Mar	70
RTTY monitor receiver			_	
K4EEU RTTV receiver demodulator for not			Dec	12
operation	p.	27,		
VILETALIVIT	p.	27,		
VE7BRK	р. р.	27, 42,	Feb	73
VE7BRK RTTY with SB-300	р. р.	27, 42,	Feb	73
VE7BRK RTTY with SB-300 W2ARZ Swap 250 CW monitor (UN)	p. p. p	27, 42, . 76,	Feb , Jul	73 68
VE7BRK RTTY with SB-300 W2ARZ Swan 350 CW monitor (HN) KIKXA	p. p. p	27, 42, 76, 63	Feb , Jul	73 68 72
VE7BRK RTTY with SB-300 W2ARZ Swan 350 CW monitor (HN) KIKXA Transceiver selectivity improved (I	р. р. р. р.	27, 42, . 76, 63,	Feb Jul	73 68 72
VE7BRK RTTY with SB-300 W2ARZ Swan 350 CW monitor (HN) KIKXA Transceiver selectivity improved (I VE3BWD	p. p. p. p. p. p.	27, 42, 76, 63, 74,	Feb Jul Jun Oct	73 68 72 70
VE7BRK RTTY with SB-300 W2ARZ Swan 350 CW monitor (HN) KIKXA Transceiver selectivity improved (I VE3BWD Tuner overload, eliminating (HN)	p. p. p. p. p. p.	27, 42, . 76, 63, 74,	Feb Jul Jun Oct	73 68 72 70
VE7BRK RTTY with SB-300 W2ARZ Swan 350 CW monitor (HN) KIKXA Transceiver selectivity improved (I VE3BWD Tuner overload, eliminating (HN) VE3GFN Attenuators for (letter)	p. p. p. p. p. p. p. p.	27, 42, . 76, 63, 74, 66,	Feb Jul Jun Oct Jan	73 68 72 70 73 74
VE7BRK RTTY with SB-300 W2ARZ Swan 350 CW monitor (HN) KIKXA Transceiver selectivity improved (I VE3BWD Tuner overload, eliminating (HN) VE3GFN Attenuators for (letter) Two-band novice superhet	p. p. p. p. p. p. p. p.	27, 42, 53, 74, 66, 69,	Feb Jul Jun Oct Jan Jan	73 68 72 70 73 74

Weather receiver, low-frequency W6GXN	٥.	36.	Oct	68
WWV receiver, fixed-tuned W6GXN	p.	24.	Nov	69
WWV receiver, regenerative WA5SNZ	p.	42,	Apr	73
WWV receiver, simple (HN) WA3JBN	p	. 68	, Jul	70
Short circuit WWV receiver, simple (HN)	p.	72,	Dec	70
WA3JBN WWV-WWVH, amateur applications	p. s fo	55, r	Dec	70
W3FQJ 455-kHz bfo, transistorized	р.	53,	Jan	72
W6BLZ, K5GXR 160-meter receiver, simple	p	. 12,	Jul	68
W6FPO 1.9 MHz receiver	p.	44,	Νον	70
W3TNO 7-MHz ssb receiver and transmitte	p r, s	. 6, simp	Dec le	69
VE3GSD Short circuit	р р.	. 6, 62,	Mar Dec	74 74
28-MHz superregen receiver K2ZSQ	p.	70,	Nov	68

#### vhf receivers and converters

Converters for six and two meters	, m	osfe	et	
WB2EGZ	р.	41,	Feb	71
Short circuit	p.	96,	Dec	71
Cooled preamplifier for vhf-uhf WAØRDX	p.	36	Jul	72
Fet converters for 50, 144, 220 an	d			
432 MHz				
W6AJF	р.	20,	Mar	68
Filter-preamplifiers for 50 and 144	I M	Hz		
etched				
W5KNT	p	. 6,	Feb	71
Fm channel scanner				
W2FPP	p.	29,	Aug	71
Fm communications receiver, mod	dula	ir .		
K8AUH	р.	32,	Jun	69
Correction	р.	71,	Jan	70
Fm receiver frequency control (let	ter)			
W3AFN	р.	65.	Apr	/1
Fm receiver performance, compar	ISO	1 of		-
VETABK	р.	68,	Ang	72
Fm receiver, multichannel for six	and	two	) 	
	р.	54,	reb	/4
KONTIL	~	24	Nov	71
For receiver unit	μ.	34,	NUV	
WA2GOF	n	6	Nov	72
Em repeaters, receiving system	P	. 0,	1101	12
degradation in				
K5ZBA	D.	36,	May	69
HW-17A, perking up (HN)				
WBEGZ	p.	70,	Aug	70
Interdigital preamplifier and comb	p-lin	е	-	
bandpass filter for vhf and uhf				
W5KHT	р	. 6,	Aug	70
Interference, scanning receiver (H	N)			
К2ҮАН	p.	70,	Sep	72
Monitor receivers, two-meter fm				
WB5EMI	p.	34,	Apr	74
Overload problems with vhf conve	rte	ſS,		
solving	_	50		• •
WIUOP Resilier allermant techniques, ut	.p.	ວ3,	Jan	/3
Keceiver augnment techniques, vn	1.11	1.4	A~	75
Receiver modular two meter fm	μ.	14,	Aug	75
WA2GFB	n.	42	Feb	72
Receiver whf fm	μ.	,		
WA2GCF	p	. 8.	Nov	75
Scanning receiver for vhf fm, impl	rove	ed '		
WA2GCF	р.	26,	Nov	74
Scanning receiver modifications,				
vhf fm (HN)				
WA5WOU	р.	60.	Feb	74

Scanning receivers for two-meter	fm			
K4IPV Six-meter converter improved	p.	28,	Aug	74
K1BQT	p.	50,	Aug	70
WB2EGZ	p.	22,	Jun	68
Squelch-audio amplifier for fm red	p. ceiv	34, ers	Aug	74
Ssb mini-tuner	р. Б	16	Oct	70
Two-meter converter, 1.5 dB NF	р. –	14	1	69
Two-meter mosfet converter	- -	. 14	, Jui	60
Neutralizing	р. р.	22, 77,	Oct	68
Two-meter preamp, MM5000 W4KAE	p.	49,	Oct	68
Vhf converter performance, optimizing (HN)		10	11	60
Vhf fm receiver (letter)	p	. 18,		68
K8IHQ Vhf receiver scanner	p.	76,	Мау	73
K2LZG Vhf superregenerative receiver, lo	р. w-v	22, oltas	Feb	73
WA5SNZ Short sircuit	Р	22,	Jul Mar	73 74
28-30 MHz preamplifier for satellit	te.	04,	war	/4
W1JAA	p.	48,	Oct	75
WA2GCF	p.	46,	Jan	73
144-MHz converter (HN) KØVQY	p.	71,	Aug	70
144-MHz converter (letter) WØLER	D.	71.	Oct	71
144 MHz converter, hot-carrier dic K8CJU	de	6.	Oct	69
144-MHz converter, modular W6110V	- -	64	Oct	70
144 MHz converters, choosing fets	s fo	r (H	N)	.0
144-MHz preamp, super (HN)	р.	70,	Aug	69
K6HCP 144-MHz preamplifier, Improved	р.	72,	Oct	69
WA2GCF Added notes	р. р.	25, 73,	Mar Jul	72 72
220-MHz mosfet converter WB2FG7	n	28	lan	69
Short circuit	р. р.	76,	Jul	69
K6JC	p.	34,	Oct	70
WA6SXC	p.	18,	May	68
W1DTY	p.	66,	Aug	<b>6</b> 9
WA2GCF	er p.	40,	Jul	75
1296-MHz converter, solid-state VK4ZT	p	6,	Nov	70
1296 MHz, double-balanced mixers WA6UAM	i fo	r - 8	hui	75
1296-MHz preamplifier	_ '	12	Oct	75
1296-MHz preamplifier, low-noise	р. 	42, EC	000	75
Added note (letter)	р. р.	50, 65,	Jan	71 72
2340-MHz converter, solid-state K2JNG, WA2LTM, WA2VTR	p.	16,	Mar	72
2304-MHz preamplifier, solid-state WA2VTR	D	20.	Auø	72
	μ.			

#### receivers and converters, test and troubleshooting

Receiver alignment		-	
Allen p.	64,	Jun	68
Rf and i-f amplifiers, troubleshooting			
Allen p.	60,	Sep	70

Signal injection in ham receivers

Allen	р.	12,	may	68
Signal tracing in ham receivers			-	
Allen	p.	52,	Apr	68
Weak-signal source, variable-outp	but			
KEJYO	р.	36,	Sep	71
Weak-signal source, 144 and 432	MH	z		
K6JC	р.	58,	Mar	70
Weak-signal source, 432 and 129	6 M I	Ηz		
K6RIL	р.	20,	Sed	68

#### p. 20, Sep 68

#### RTTY

AFSK generator, crystal-controlled	1			_
K7BVT	P	. 13,	Jul	72
AFSK generator, crystal-controlle	d		_	
W6LLO	р.	14,	Dec	73
Sluggish oscillator (letter)	p.	59,	Dec	74
WAAEGY	-	20	0.4	60
Audio-frequency kever simple	μ.	20,	UCL	00
W2ITI		56	Διισ	75
Audio-shift kever, continuous-pha	se.	50,	Aug	,,,
VE3CTP		10.	Oct	73
Short circuit	p.	64,	Mar	74
Automatic frequency control for				
receiving RTTY				
W5NPO	р.	50,	Sep	71
Added note (letter)	p.	66,	Jan	72
Autostart, digital RTTY		-		_
K4EEU	F	<b>).</b> 6,	Jun	73
Autostart monitor receiver		~ 7	_	-
CRT intensifier for RTTY	р.	37,	Dec	72
	-	10	11	71
Carriage return adding to the aut	ч С	. 10, atio	Jui	/1
line-feed generator (HN)	UIII	anc		
K4FFU	п	71	Sen	74
Coherent frequency-shift keving, n	eec	i for	oop	
K3WJQ	p.	30,	Jun	74
Added notes (letter)	р.	58,	Nov	74
Crystal test oscillator and signal				
generator				
K4EEU	р.	46,	Mar	73
CW memory for RTTY identificatio	n	_		
WELLO	<u>٦</u>	). 6,	Jan	74
Electronic speed conversion for R	IIY			
teleprinters	_	20	<b>n</b>	-7.1
WADJIJ Brinted circuit for	р.	30,	Dec	71
Frequency-shift meter RTTY	р.	54,	001	12
VK3ZNV	р.	53.	Jun	70
Line-end indicator, IC	<b>P</b>	,	• • • •	
W2OKO	р.	22,	Nov	75
Line feed, automatic for RTTY				
K4EEU	р.	20,	Jan	73
Mainline ST-5 autostart and antisp	pace	e	_	
KZYAH	р.	46,	Dec	12
Wannine SI-5 KIIT demodulator	-	14	S	70
Short circuit	р. р	72	Dec	20
Mainline ST-6 RTTY demodulator	μ.	12,	Dec	10
W6FFC	п	6.	Jan	71
Short circuit	р.	72.	Anr	71
Mainline ST-6 RTTY demodulator.	mo	re		• •
uses for (letter)				
W6FFC	p.	69,	Jul	71
Mainline ST-6 RTTY demodulator,				
troubleshooting				
W6FFC	р.	50,	Feb	71
Message generator, random acces	s m	emo	ry	
RTTY		~		
K4EEU	р	. 8,	Jan	75
Wessage generator, RITY	_	20	<b>5</b> - 1	74
Monitor soons share shift	р.	30,	rep	/4
Wanty wanty		26	A	70
Manitar soors DTTV Hast	р.	30,	ĸug	12
HO-10 and SR-610 ac (HN)				
KOHAM		70	Sor	71
	μ.	<i>, ,</i>	uch.	/ **

Monitor scope, RTTY, solid-state WB2MPZ	p.	33,	Oct	71
Phase-locked loop AFSK generator	· _			77
Phase-locked loop RTTY terminal	p. uni	τ, t	mar	13
W4FQM Correction	្ត	5. 8,	Jan	72
Power supply for	р. р	. 60	. Jul	74
Optimization of the phase				
locked terminal unit Precise tuning with sch gear	ρ.	22,	Sep	75
WØKD	p,	40,	Oct	70
Printed circuit for RTTY speed cor	ve	rter	~	70
Receiver-demodulator for RTTY ne	p. t	54,	Uct	12
operation				
VE7BRK Pibbon re-inkers	<b>р</b> .	42,	Feb	73
W6FFC	p.	30,	Jun	72
RTTY converter, miniature IC				~~
Short circuit	р. п.	40, 80.	Aug	69 69
RTTY distortion: causes and cures		,		•
WB6IMP BTTY for the blind (letter)	p.	36,	Sep	72
VE7BRK	р.	76,	Aug	72
RTTY, introduction to	•	38	lun	69
RTTY line-length indicator (HN)	μ.	50,	Jun	0.5
W2UVF	p.	62,	Nov	73
KITT reception with Heath 3B rec K9HVW	p.	64,	Oct	71
RTTY with the SB-300		~~		~~
WZARZ Signal Generator, RTTY	P	. 76	, JUI	68
W7ZTC	p.	23,	Mar	71
Short circuit Speed control electronic for BTT	p.	96,	Dec	71
W3VF	р.	50,	Aug	74
ST-5 keys polar relay (HN)	_	70		74
Swan 350 and 400 equipment on :	ים. דז	ΓΥ (H	HN)	/4
WB2MIC	р.	67,	Aug	69
W6FOO	D.	30.	Dec	70
Synchrophase RTTY reception				
W6F00 Teleprinters new look in	p.	38,	Νον	70
W6JTT	р	. 38	, Jul	70
Terminal unit, phase-locked loop			1	72
Correction	р.	60,	Jan May	72
Terminal unit, phase-locked loop	•			
W4AYV Terminal unit, variable-shift RTTY	p.	36,	Feb	/5
W3VF	p.	16,	Nov	73
Test generator, RTTY (HN) W3EAG	р.	67,	Jan	73
Test generator, RTTY (HN) W3EAG	D.	59	Mar	73
Voltage supply, precision for	۳.	,		
phase-locked terminal unit (HN) WA6TLA	n	. 60		74
· · · · · · · · · · · · · · · · · · ·	۲		,	

## satellites

apny			
р.	60,	Aug	68
p	. 77,	Oct	68
nuth	/elev	atior	1
p.	26,	Jan	75
p,	58,	Dec	75
p.	59,	Feb	75
р.	24,	May	74
p.	34,	Mar	75
	pny p. p. p. p. p. p. p.	p. 60, p. 77, nuth/elev p. 26, p. 58, p. 59, p. 24, p. 34,	pp. 60, Aug p. 77, Oct nuth/elevation p. 26, Jan p. 58, Dec p. 59, Feb p. 24, May p. 34, Mar

Circularly-polarized ground-plane antenna for satellite communic	ations
K4GSX	p. 28, Dec 74
Communications, first step to sal	ellite
KIMTA	p. 52, Nov 72
Added notes (letter)	p. 73, Apr 73
Oscar 7, communications techniq	ues for
G3ZCZ	p. 6, Apr 74
Picture transmission, recording s	atellite
W6CCN	p. 6, Nov 68
Signal polarization, satellite	
кныј	p. 6, Dec 72
28-30 MHz preamplifier for satelli reception	ite
W1JAA	p. 48, Oct 75
432-MHz OSCAR antenna (HN)	
WIJAA	p. 58, Jul 75

#### semiconductors

Antenna switch for meters, solid-s K2ZSQ	tat p.	e 48,	Мау	69
Avalanche transistor circuits W4NVK	p.	22,	Dec	70
Beta master, the K8ERV	D.	18.	Aug	68
Charge flow in semiconductors	n	50	Anr	7)
Converting a vacuum-tube receive	r to	s <sup>30</sup> ,	λφ.	
W100P	p.	26,	Feb	69
Short circuit Converting vacuum tube equipmer	p ht t	. 76 :0	, JUI	69
solid-state	_	20	A	60
Curve master, the	р.	30,	MUB	
K8ERV Diodes, evaluating	p.	40,	Mar	68
W5JJ	р.	52,	Dec	71
VE7ABK	p.	65,	Oct	71
Fet bias problems simplified WA5SNZ	p.	50,	Mar	74
Fet biasing W3FO1	р.	61.	Nov	72
Fetrons, solid-state replacements f	or	tube	s	70
Added notes p. 66, Oct 73;	р р.	62,	Jun	74
Frequency multipliers W6GXN	р	. 6,	Aug	71
Frequency multipliers, transistor W6AJF	р.	49,	Jun	70
Glass semiconductors W1EZT	p	54	, Jul	69
Grid-dip oscillator, solid-state conv W6AJZ	ers D.	ion 20.	of Jun	70
Heatsink problems, how to solve t	ran	sist	or	74
Impulse generator, snap diode	р. _	40,	Jan	74
Injection lasers, high power	p.	29,	UCI	12
Mims Injection lasers (letter)	p.	28,	Sep	71
Mims	p.	64,	Apr	71
Chambers	rso p	. 6,	Aug	74
Linear transistor amplifier W3FQJ	р.	59,	Sep	71
Long-tail transistor biasing W2DXH	ю.	64.	Apr	68
Mobile converter, solid-state modif	fica	tion 58.	of Sen	69
Mosfet circuits		,		70
W3FQJ Mosfet transistors (HN)	р.	50,	red	/ 5
WB2EGZ Motorola fets (letter)	p.	72,	Aug	69
WICER	p.	64,	Apr	71
Motorola MPS transistors (HN) W2DXH	р.	42,	Apr	68

Neutralizing small-signal amplifier	rs D	40	Sen	70
Noise, zener-diode (HN)	<b>_</b>	50		75
Parasitic oscillations in high-powe	r <sup>p.</sup>	55,	50.1	75
transistor if amplifiers WØKGI	р.	54,	Sep	70
Pentode replacement (HN) W1DTY	р.	70,	Feb	70
Power dissipation ratings of trans WN9CGW	isto p.	ors 56,	Jun	71
Power fets W3FOJ	n	34	Anr	71
Power transistors, parallelling (HN	ເ)ຼົ	62	120	72
Relay, transistor replaces (HN)	μ.	70	Jan	70
Replace the unijunction transistor	р.	12,	Jan	/0
K9VXL Rf power detecting devices	р.	58,	Apr	68
K6JYO Rf power transistors, how to use	ρ.	28,	Jun	70
WA7KRE Snan diode impulse generator	F	o. 8,	Jan	70
Siegal, Turner	p.	29,	Oct	72
W2FPP	p.	38,	Dec	70
WA7KRE	p.	54,	Oct	70
Transconductance tester for field- transistors	effe	ct		
W6NBI Transistor amplifiers, tabulated	р.	44,	Sep	71
characteristics of W511	n	зn	Mar	71
Transistor and diode tester	, .	65	Nov	70
Transistor breakdown voltages	μ.	05,		70
WASEKA Transistors for vhf transmitters (H	р. (N)	44,	Feb	/5
W100P Transistor storage (HN)	р.	74,	Sep	69
K8ERV Transistor tester	p.	58,	Jun	68
WA6NIL Transistor tester for leakage and	p	. 48	, Jul	68
W4BRS	p.	68,	May	68
Allen	p	. 62	Jul	70
Transistor-tube talk (HN) WA4NED	p.	25,	Jun	68
Trapatt diodes (letter) WA7NLA	р.	72,	Apr	72
Troubleshooting around fets Allen	D.	42.	Oct	68
Troubleshooting transistor ham ge Allen	ar	64	Ind	68
Vfo transistors (HN)	~	74	Nov	60
Y parameters in rf design, using	<b>ب</b>	/ <del>4</del> ,	1	70
Zener diodes (HN)	p	. 40,	Jut	12
K3DPJ Zener tester, Low voltage (HN)	р.	79,	Aug	68
КЗДЪЛ	ρ.	72,	Nov	69

### single sideband

Balanced modulator, integrated-c	ircu	it		
K7QWR	p	. 6,	Sep	70
Balanced modulators, dual fet				
W3FQJ	D.	63.	Oct	71
Communications receiver, phasin	g∙ty	pe		
WAØJYK	P	. 6,	Aug	73
Converting a-m power amplifiers ssb service	to		-	
WA4GNW	p.	55,	Sep	68
Converting the Swan 120 to two i	nete	ers		
K6RIL	p.	8,	May	68
Detectors, ssb				
Belt	p.	22,	Nov	68

Detector, ssb, IC (HN)	
K4ODS	p. 67, Dec 72
Correction Double balanced mixers	p. /2, Apr /3
WIDTY Double-balanced modulator, broa	p. 48, Mar 68 adband
WA6NCT	p. 8, Mar 70
Electronic bias switching for line amplifiers	ar 50 M 7r
Filters, single-sideband	p. 50, Mar /:
Belt Filters, ssb (HN)	p. 40, Aug 68
K6KA Frequency dividers for ssh	p. 63, Nov 73
W7BZ Frequency translation in ssb	p. 24, Dec 71
transmitters Belt	p. 22, Sep 68
Generating ssb signals with suppressed carriers	
Belt Guide to single sideband, a beginner's	р. 24, Мау 68
Belt Hang agc circuit for ssb and CV	p. 66, Mar 68 √
WIERJ	p. 50, Sep 72
W6SAI Intermodulation-distortion measured	p. 24, Jan 71 p. 25, Jan 71 urements
on ssb transmitters W6VFR	p. 34, Sep 74
Linear amplifier, five-band condu cooled	uction-
Linear amplifier, five-band kilowa	p. 6, Jul /2 att p. 14 Jon 74
Improved operation (letter) Linear amplifier, homebrew five-	p. 14, Jan 74 p. 59, Dec 74 band
W7IV	p. 30, Mar 70
Unear amplifier performance, in W4PSJ	p. 68, Oct 71
W6WR	p. 28, Dec 75
Linear, five-band hf W7D1	p. 6, Mar 72
Linear for 80-10 meters, high-po- W6HHN	wer n. 56. Apr 71
Short circuit	p. 96, Dec 71
Linear power amplifiers	n 16 Apr 68
Linears, three bands with two (H	1N) = 70 New 60
Minituner, ssb	p. 70, NOV 89
K1BQT Modifying the Heath SB-200 amp	p. 16, Oct 70 olifier
W6UOV	p. 32, Jan 71
Belt	p. 26, Jun 68
Peak envelope power, how to me W5.U	asure n 32. Nov 74
Phase-shift networks, design crit G3NRW	eria for p. 34, Jun 70
Phase-shift ssb generators Belt	p. 20, Jul 68
Power supplies for ssb Belt	p. 38, Feb 69
Precise tuning with ssb gear WØKD	p. 40, Oct 70
Pre-emphasis for ssb transmitter OH2CD	rs p. 38, Feb 72
Rating tubes for linear amplifier W6UOV, W6SAI	service p. 50, Mar 71
Kt cupper for the Collins S-line K6JYO Letter	p. 18, Aug 71
Rf speech processor, ssb	p. 00, Dec 71
W2MB Sideband location (HN)	p. 18, Sep 73
NUNA	p. oz, Aug /3

Solid-state circuits for ssb				
Belt Solid-state transmitting converter 144-MHz ssb	p. for	18,	Jan	69
W6NB1 Short circuit	p.	6, 6, 62.	Feb Dec	74 74
Speech clipper, IC K6HTM	р.	18,	Feb	73
Added notes (letter) Speech clipper, rf, construction	р.	64,	Oct	73
G6XN Speech clippers, rf, performance o	p. of	12,	Dec	72
G6XN Added notes p. 58, Aug 73; Speech clipping	р. р.	26, 72,	Nov Sep	72 74
K6KA Speech clipping in single-sideband	p. ec	24, Juipi	Apr ment	69
K1YZW Speech processing	р.	22,	Feb	71
W1DTY Speech processing, principles of	p.	60,	Jun	68
ZLIBN Added notes p. 75, May 75; Speech processor for ssh	р. р.	28, 64,	Feb Nov	75 75
K6PHT Speech process logarithmic	p.	22,	Apr	70
WA3FIY Speech processor, ssb	p.	38,	Jan	70
VK9GN Speech splatter on single sideband	р.	31,	Dec	71
W4MB Ssh exciter 5-band	, р.	28,	Sep	75
K1UKX Ssb. generator, phasing-type	p.	10,	Mar	68
W7CMJ Added comments (letter)	р. <b>р</b> .	22, <b>65,</b>	Apr Nov	73 73
W9KIT	P	. 6,	Dec	70
Witching and linear amplification W3FQJ	р.	61,	Oct	71
Transceiver, miniature 7-MHz W7BBX	p.	16,	Jul	74
Transceiver, single-band ssb W1DTY	р	. 8,	Jun	69
Transceiver, ssb, IC G3ZVC Circuit change (letter)	p.	34, 62	Aug	74 75
Transceiver, ssb, using LM373 IC W5BAA	р. р.	32,	Nov	73
Transceiver, 3.5-MHz ssb VE6ABX	, D	. 6,	Маг	73
Transmitter alignment Allen	р.	62.	Oct	69
Transmitter and receiver for 40 me	ete	s, s 6.	sb Mar	74
Short circuit Transmitter phasing-type ssb	p.	62,	Dec	74
WAØJYK Transmitting mixers 6 and 2 mete	p	. 8,	Jun	75
K2ISP Transverter 6-meter	p	. 8,	Apr	69
K8DOC, K8TVP	p.	44,	Dec	68
VE3CUS	p.	22,	Dec	69
G4ADJ Tuning un seb transmitters	р.	18,	Νον	<b>7</b> 5
Allen TV sween tubes in linear service	p.	62,	Nov	69
full-blast operation of		. 9,	Apr	68
1100/11, 1100/01	P			
Two-tone oscillator for ssb testing W6GXN	р.	11,	Apr	72
Woorn, wood for ssb testing W6GXN Vacuum tubes, using odd-ball type linear amplifier service W5JJ	р. si s.	11, n 58.	Apr Sed	72 72
Two-tone oscillator for ssb testing W6GXN Vacuum tubes, using odd-ball type linear amplifier service W5JJ Vhf, uhf transverter, input source F8MK	p. si p. for	11, n 58, (HN 69.	Apr Sep I) Sep	72 72 72 70
Two-tone oscillator for ssb testing W6GXN Vacuum tubes, using odd-ball type linear amplifier service W5JJ Vhf, uhf transverter, input source F8MK Vox and mox systems for ssb Belt	p. si p. for p. p.	11, n 58, (HN 69, 24,	Apr Sep I) Sep Oct	72 72 70 68

Vox, versatile		
W9KIT	p. 50, Jul	71
Short circuit	p. 96, Dec	71
3-500Z in amateur service, the		
W6SAI	p. 56, Mar	68
144-MHz linear, 2kW	-	
W6UOV, W6ZO, K6DC	p. 26, Apr	70
144-MHz low-drive kilowatt linear		
W6HHN	p. 26, Jul	70
144-MHz transverter, the TR-144		
KIRAK	p. 24, Feb	72
432 MHz rf power amplifier		
Kejc	p. 40, Apr	70
432-MHz ssb converter		
Kejc	p. 48, Jan	70
Short circuit	p. 79, Jun	70
432-MHz ssb, practical approach	to	
WAZESQ	p. 6, Jun ;	71
1296-MHZ SSD transceiver		~ .
WASUAM	p. 8, Sep 1	74

### television

Camera and monitor, sstv		
VE3EGO, Watson	p. 38, Apr	69
Color tv. slow-scan		
W4UMF, WB8DQT	p. 59, Dec	69
Computer, processing, sstv pictur	es	
W4UMF	p. 30, Jul	70
Fast-scan camera converter for ss	tv	
WA9UHV	p. 22, Jul	74
Fast- to slow-scan conversion, tv		
W3EFG, W3YZC	p. 32, Jul	71
Frequency selective and sensitivity	/-	
controlled sstv preamp	<b>AC 1</b> 1	
DKIBF	p. 36, Nov	/5
Slow-scan television	- 50 5	~~
WAZENIC	p. 52, Dec	63
Sync generator, IC, for ATV	- 24 I.J.	75
www.kgi Synab ganarator acts (lattar)	p. 34, Jui	15
Wills	n 73 Anr	72
Television DY	P. 75, Apr	/5
WA9RAO	n 30 Aug	73
Test generator, sstv	P. Col Mug	
K4EEU	D. 6. Jul	73
		• •

# transmitters and power amplifiers

#### general

Amplitude modulation, a different WA5SNZ	ар р.	proa 50,	ch Feb	70
Batteries, how to select for portab equipment	le			
WAØAIK	р.	40,	Aug	73
Blower maintenance (HN) W6NIF	р.	71,	Feb	71
Blower-to-chassis adapter (HN) K6JYO	р.	73,	Feb	71
Converting a-m power amplifiers t ssb service	0			
WA4GNW	р.	55,	Sep	68
Efficiency of linear power amplifie how to compare	rs,			
W5JJ	р	64	Jul	73
Electronic bias switching for linea amplifiers	r			
WOVFR	p.	50,	Mar	75
Fail-safe timer, transmitter (HN) K9HVW	р.	72,	Oct	74
Filters, ssb (HN)	_	£ 2	Nov	72
RONA Executional multiplicate	μ.	63,	NUV	/3
W6GXN	Р	. 6,	Aug	71

Frequency translation in ssb	
Transmitters Belt	n 22 Sen 68
Grid-current measurement in	p. 22, 00p 00
grounded-grid amplifiers	
W6SAI	p. 64, Aug 68
tubes	ower
W6SAI	p. 24, Jan 71
Key and vox clicks (HN)	
	p. 74, Aug 72
Belt	p. 16. Apr 68
Lowpass filters for solid-state line	ear amplifiers
WAØJYK	p. 38, Mar 74
Short circuit	p. 62, Dec 74
Wittiple tubes in parallel ground W7CSD	ng gria (HN) n 60. Aug 71
Networks, transmitter matching	p. 66, Mug / 1
W6FFC	p. 6, Jan 73
Neutralizing tip (HN)	- 60 Dec 70
Parasitic oscillations in high-now	p. 69, Dec 72
transistor rf amplifiers	
WØKGI	p. 54, Sep 70
Parasitic suppressor (HN)	70
Pi and Pi-L networks	p. 80, Apr 70
W6SAI	p. 36. Nov 68
Pi network design aid	•
W6NIF	p. 62, May 74
Pinetwork design high-frequency	p. 56, Dec 74
power amplifier	
W6FFC	p. 6, Sep 72
Pi-network inductors (letter)	- 79 0 72
Pi networks, series tuned	p. 78, Dec 72
W2EGH	p. 42, Oct 71
Power attenuator, all-band 10-dB	
KICCL Power fets	p. 68, Apr 70
W3FQJ	p. 34, Apr 71
Power tube open filament pins (H	IN)
W9KNI	p. 69, Apr 75
OH2CD	ь р. 38. Feb 72
Relay activator (HN)	p. 00, 100 / 1
КбКА	p. 62, Sep 71
Rf power amplifiers, high-efficien	
Rf power transistors, how to use	p. 0, 001 /4
WA7KRE	p. 8, Jan 70
Screen clamp, solid-state	
WØLRW Step-start circuit bigh-voltage (H	p. 44, Sep 68
W6VFR	p. 64, Sep 71
Swr alarm circuits	• • •
W2EEY	p. 73, Apr 70
Temperature alarms for high-pow W2FFY	n. 48. Jul 70
Transmitter power levels, some	p. 40, 541 70
observations regarding	
WA5SNZ	p. 62, Apr 71
Transmitter, remote keying (HN)	n 74 Oct 69
Transmitter switching, solid-state	p. 14, oct 05
W2EEY	p. 44, Jun 68
Transmitter-tuning unit for the bl	ind
W9NTP	p. 60, Jun 71
iv sweep tubes in linear service, full-blast operation of	
W6SAI, WEUOV	p. 9, Apr 68
Vacuum tubes, using odd-ball typ	es in
linear amplifiers	n 58 San 72
Vfo. digital readout	p. 30, 3ep /2
WB8IFM	p. 14, Jan 73

#### high-frequency transmitters

ART-13, Modifying for noiseless C K5GKN	W( р.	HN) 68,	Aug	69
CW transceiver for 40 and 80 met W3NNL, K3OIO	ers	14	. Jul	69
CW transceiver, low-power 20-mete	er	ς Ω	Nov	74
CW transmitter, half-watt	р	. 0,	NUV	/4
KØVQY Driver and final for 40 and 80 me	p. ters	69, 5,	Nov	69
solid-state W30B0	n	20	Feh	72
Field-effect transistor transmitters	p.	20,		71
Filters, low-pass for 10 and 15 me	p. ter:	30, 5	reo	/1
W2EEY Frequency synthesizer, high frequ	р. enc	42, y	Jan	72
K2BLA Grounded-grid 2 kW PEP amplifier	р.	16,	Oct	72
high frequency		¢	Fab	60
Heath HW-101 transceiver, using v	р with	. <b>0</b> , 1	reo	69
a separate receiver (HN)		~~	<b>.</b>	-
Linear amplifier, five-band	р.	63,	UCT	/3
W/IV Linear amplifier, five-band conduc	р. tior	30, ⊪co	Mar oled	70
W9KIT	ſ	<b>b.</b> 6	, Jul	72
W4PSJ	p.	ing 68,	Oct	71
Linear amplifier, 100-watt W6WR	D.	28.	Dec	75
Linear, five-band hf		6	Mar	72
Linear, five-band kilowatt	р. 	14	lon	74
Improved operation (letter)	р. р.	59,	Dec	74 74
Linear for 80-10 meters, high-powe W6HHN	er p.	56,	Apr	71
Short circuit	p.	96,	Dec	71
solid-state				
Chambers Linears, three bands with two (HN	p.	6,	Aug	74
W4NJF	р.	70,	Nov	69
state	_	1.0	<b>N</b> 1	~~
Lowpass filter, high-frequency	р.	10,	NOV	60
W2OLU Short circuit	р.	24,	Mar	75
Modifying the Heath SB-200 ampli	p. fier	for	Jun	75
the new 8873 zero-bias triode	_	32	120	71
Phase-locked loop, 28 MHz	p.	40	Jan	7.
QRP fet transmitter, 80-meter	р.	40,	Jan	/3
W3FQJ Ssb exciter, 5-band	р.	50,	Aug	75
KIUKX Ssh transceiver miniature 7.MHz	p.	10,	Mar	68
W7BBX	p.	16,	Jul	74
W5BAA	р.	32,	Nov	73
Ssb transceiver, 9-MHz, IC G3ZVC	n.	34.	Aug	74
Circuit change (letter)	р.	62,	Sep	75
VE3GSD	p.	6,	Mar	74
Short circuit Ssb transmitter, phasing type	p.	62,	Dec	74
WAØJYK	p.	8,	Jun	75
W6SAI	1-tre P	eque ). 6,	Jul	70
Transceiver, single-band ssb W1DTY	p	8.	Jun	69
Transceiver, 3.5-MHz ssb	-	-, F	Mor	72
TLUNDA	ρ.	υ,	14161	13

Transmitter, low-power				
W6NIF	p.	26,	Dec	70
Transmitters, QRP				
W7OE	p.	36,	Dec	68
Transmitter, universal flea-power	•			
K2ZSQ	р.	58,	Apr	69
Transverter, high-level hf	•	,	•	
K4ERO	D.	. 68.	Jul	68
3-500Z in amateur service, the	•			
W6SAI	р.	56.	Mar	68
14-MHz vfo transmitter, solid-state	e			
W30B0	- D	. 6.	Nov	73
28-MHz transmitter, splid-state	۲	,		
K2ZSO	D.	10	tut	68
40-meters transistor rig for		,		
W6BLZ K5GXR	п	44	.tut	68
160-meters 500-watt power amplif	ior			
W2RP	'n	8	Aug	75
112.01	ч	,	Aug	, ,

#### vhf and uhf transmitters

Converting the Swan 120 to two n	nete	ers 8.	Mav	68
Fm repeater transmitter, improvin	ຮຼົ	24	Oct	69
Linear for 2 meters	μ.	47	Uct	~
W4KAE Linear for 1296 MHz, high-power	р.	47,	Jan	03
WB6IOM Phase-locked loop, 50 MHz	p	. 8,	Aug	68
W1KNI Transistors for vhf transmitters (h	p. IN)	40,	Jan	73
WIOOP Transmitter flag nower	p.	74,	Sep	69
K2ZSQ	p.	80,	Dec	68
K2ISP	nete P	ers . 8,	Apr	69
Transverter for 6 meters WA9IGU	p.	44	, Jul	69
Tunnel diode phone rig, 6-meter ( K27SO	HŃ) D.	74	. Jul	68
Vhf linear, 2kW, design data for	-	c .	Mar	60
50-MHz kilowatt, inductively tuned	р	. 0,	wiar	
K1DPP 50-MHz linear amplifier	p	. 8,	Sep	/5
K1RAK 50-MHz linear amplifier, 2-kW	p.	38,	Nov	71
W6UOV	р.	16,	Feb	71
W6SAI	I	p. 6	, Jul	70
WB2EGZ	¢	o. 6,	Oct	68
50-MHz transverter K1RAK	p.	12,	Mar	71
50/144-MHz multimode transmitte K2ISP	r p.	28.	Sep	70
144-MHz fm transmitter			Anr	72
144-MHz fm transmitter, solid-stat	ie P	. 0,		
W6AJF 144-MHz fm transmitter Sonobab	p. v	14	, Jui	/1
WAØUZO	, Ρ	. 8,	Oct	71
Short circuit	p.	96,	Dec	71
Crystal deck for	p.	26,	Oct	72
144-MHz low-drive kilowatt linear W6HHN	D.	26	. Jul	70
144-MHz low-power solid-state tra	nsm	nitte	r Mar	70
144-MHz phase-modulated transm	p. vitte	52, :r	war	70
W6AJF	p.	18,	Feb	70
W6UOV	пог р.	22,	Aug	71
144-MHz power amplifier, 10-watt	sol	id∙st	ate	74
144-MHz rf power amplifiers, solid	p. Ist	o/, ate	Jan	74
W4CGC	p - U -	. 6,	Apr	73
WENDI	0110	-sta	Le SS	7.4
Short circuit	р. р.	62,	Dec	74 74
	-			

144-MHz transceiver, a-m				
K1AOB	р.	55,	Dec	71
144-MHz two-kilowatt linear	-			
WEUOV, WEZO, KEDC	ם.	26,	Apr	70
144- and 432- stripline amplifier/t	ripl	er		• •
K2RIW		6.	Feb	70
220-MHz exciter				• -
WB6DJV	n.	50.	Nov	71
220-MHz power amplifier		,		• -
W6UOV	п.	44.	Dec	71
220-MHz, rf power amplifier for	μ.			
WB6DJV	σ.	44.	Jan	71
220-MHz rf power amplifier, vhf f	m			
K7JUE	D	6.	Sed	73
432-MHz amplifier, 2-kW				
W6DAI, W6NLZ	P	. 6,	Sep	68
432-MHz exciter, solid-state	•		•	
W100P	p.	38,	Oct	69
432-MHz rf power amplifier				
K6JC	р.	40,	Apr	70
432-MHz solid-state linear amplific	er			
WB6QXF	p.	30,	Aug	75
432-MHz ssb converter				
KEJC	ρ.	48,	Jan	70
Short circuit	р.	79,	Jun	70
432-MHz 100-watt solid-state power	er a	mpl	fier	_
WA7CNP	p.	36,	Sep	75
1296-MHz frequency tripler				
K4SUM, W4API	р.	40,	Sep	69
1296-MHz power amplifier				
W2COH, W2CCY, W2OJ,		40		
WINU CONTRACTOR	р.	43,	Mar	70
2304-MHz power amplifier		•	<b>F</b> - 1-	76
WASHUV	p	. В,	rep	15

•

#### transmitters and power amplifiers, test and troubleshooting

Aligning vhf transmitters Allen	p. 58, Sep 68
Ssb transmitter alignment Allen	p. 62, Oct 69
Transverter, 6-meter K8DOC, K8TVP	p. 44, Dec 68
Tuning up ssb transmitters Allen	p. 62, Nov 69

### troubleshooting

Analyzing wrong dc voltages Allen	p.	54,	Feb	69
Audio distortion, curing in speech				
amplifiers			A	70
De de convertere ouring trouble in	р.	42,	Aug	/0
Allen	р.	56.	Jun	70
Fets, troubleshooting around		•		
Allen	p.	42,	Oct	68
High-voltage troubleshooting				
Allen	p.	52,	Aug	68
Mobile power supplies, troublesho	otir	١g	_	
Allen	р.	56,	Jun	70
Ohmmeter troubleshooting				
Allen	р.	52,	Jan	69
Oscillators, repairing				
Allen	p.	69,	Mar	70
Oscilloscope, putting to work				
Allen	p.	64,	Sep	69
Oscilloscope, troubleshooting ama	teu	r		
gear with				
Allen	р.	52,	Aug	69
Receiver alignment				
Allen	р.	64,	Jun	68
Receiver alignment techniques, vh	f fr	n	_	
K4IPV	р.	14,	Aug	75
Resistance measurement, troubles	hoo	oting	by	
Allen	р.	62,	Nov	68

Rf and i-f amplifiers, troubleshoot	ing			
Allen	р.	60,	Sep	70
Signal injection testing in receiver	rs –			
Allen	р.	72,	May	68
Signal tracing in amateur receiver	rs -			
Allen	p.	52,	Apr	68
Speech amplifiers, curing distortle	on			
Allen	р.	42,	Aug	70
Ssb transmitter alignment				
Allen	p.	62,	Oct	69
Sweep generator, how to use				
Allen	р.	60,	Apr	70
Transistor amateur gear, troubles	100	ting		
Allen	р	. 64,	Jul	68
Transistor testing				
Allen	р	. 62,	Jul	70
Tuning up ssb transmitters				
Allen	р.	62,	Nov	69
Vhf transmitters, aligning				
Allen	p.	58,	Sep	68

### vhf and microwave

#### general

Amateur vhf fm operation W6AYZ	р. 36, Јип 68
scattering characteristics	B 18 Nov 74
A-m modulation monitor (HN)	p. 18, NOV 74
K7UNL APX-6 transponder notes on	p. 67, Jul 71
W60SA	p. 32, Apr 68
Band change from six to two meters	ers, quick n. 64. Feb 70
Bandpass filters, single-pole	n. 51 Sep 69
Bandpass filters, 25 to 2500 MHz	p. 61, Sep 69
Bypassing, rf, at vhf	p. 40, Sep 09
WB6BHI Cavity filter 144-MHz	p. 50, Jan 72
WISNN	p. 22, Dec 73
Short circuit	p. 64, Mar 74
Coaxial filter, vhf W6SAI	p. 36 Aug 71
Coaxial-line resonators (HN)	p. 00, nug /1
WA7KRE Coll-winding data practical vbf an	p. 82, Apr 70
K3SVC	p. 6, Apr 71
Crystal mount, untuned	n 69 Jun 69
Effective radiated power (HN)	p. 66, Juli 66
VE7CB	p. 72, May 73
W6GXN	p. 6, Aug 71
W6AJF	p. 49, Jun 70
Frequency scaler, 500-MHz W6URH	p. 32. Jun 75
Frequency scalers, 1200-MHz	
Frequency synchronization for	p. 38, Feb /5
scatter-mode propagation	- 06 Gan 71
Frequency synthesizer, 220 MHz	p. 26, Sep /1
W6GXN	p. 8, Dec 74
W6UOV	p. 8, Jan 69
Harmonic generator (HN)	p 76 Oct 70
Impedance bridge (HN)	p. 70, 000 70
W6KZK Indicator sensitive rf	p. 67, Feb 70
WB9DN1	p. 38, Apr 73
Klystron cooler, waveguide (HN) WA4WDL	p. 74, Oct 74
Lunar-path nomograph WA6NCT	p. 28. Oct 70

Microwave communications, ama standards for	teur
КбНЦ	p. 54. Sep 69
Microwave hybrids and couplers	for amateur use
W2CTK	p. 57, Jul 70
Short circuit	p. 72. Dec 70
Microwaves, getting started in	
Roubal	p. 53, Jun 72
Microwaves, introduction to	•
W1CBY	p. 20, Jan 72
Moonbounce to Australia	•
WIDTY	p. 85, Apr 68
Noise figure, meaning of	
K6MIO	p. 26, Mar 69
Noise figure measurements, vhf	
WB6NMT	p. 36, Jun 72
Noise generators, using (HN)	
K2ZSQ	p. 79, Aug 68
Phase-locked loop, tunable 50 MH	١z
WIKNI	p. 40, Jan 73
Power dividers and hybrids	
WIDAX	p. 30, Aug 72
Proportional temperature control	for crystal
ovens	
VEDEP Dedia absorvatory, whf	p. 44, Jan 70
Ham	- 44 Jul 74
Deflex klystrons nore stick for (I	µ, ui /4
W68PK	אור) די 10, 11 מי
Rf nower-detecting devices	p. /1, Jul /J
K61YO	p 28. Jup 70
Satellite communications	p. 20, 300 70
KITMA	n. 52. Nov 72
Added notes (letter)	p. 73, Apr 73
Satellite signal polarization	• • •
KH6IJ	p. 6, Dec 72
Solar cycle 20, vhfer's view of	
WASIYX	p. 46, Dec 74
Tank circuits, design of vhf	
	p. 56, Nov 70
Unt nardware (HN)	- 76 0-1 70
Via high stability whi	p. 76, Uct 70
	n 27 Jan 72
Vhf beacons	p. 27, Jan 72
KAEDX	n 52 Oct 69
Vhf beacons	p. 52, 661 65
W3FOJ	n. 66. Dec 71
50-MHz frequency synthesizer	p,
W1KNI	p. 26. Mar 74
144-MHz fm frequency meter	p ,
W4JAZ	p. 40, Jan 71
Short circuit	p. 72, Apr 71
144-MHz frequency synthesizer	
WB4FPK	p. 34, Jul 73
144-MHz frequency-synthesizer, o	ne-
220 MHz frequency cynthesizer	p. 30, Sep /3
W6GXN	n 8 Dec 74
432-MHz ssb. practical approach	to p. 0, 000 74
WA2FSO	. 6. Jun 71
1296 MHz microstripline bandpas	s filters
WAGUAM	p. 46, Dec 75
40-GHz record	
K7PMY	p. 70, Dec 68

## vhf and microwave antennas

Circularly-polarized ground-plane antenna for satellite communications K4GSX p. 28, Dec 74 Ground plane, portable vhf (HN) K9DHD p. 71, May 73 Log-periodic yagi beam antenna K6RIL, W6SA! p. 8, Jul 69 Correction p. 68, Feb 70 Microstrip swr bridge, vhf and uhf W4CGC p. 22, Dec 72

Microwave antenna, low-cost	n.	52.	Nov	69
Parabolic reflector antennas	р. -	12	May	74
Parabolic reflector element spacir	p. Ig	12, 20	May	74
Parabolic reflector gain	р.	28,	may	75
W21QK Parabolic reflector, 16-foot homeb	p rev	. 50 V	, Jul	/5
WB6IOM Parabolic reflectors, finding	p	o. 8,	Aug	69
focal length of (HN) WA4WDL	p.	57,	Mar	74
Swr meter W6VSV	ı	o. 6,	Oct	70
Transmission lines, uhf WA2VTR	p.	36,	May	71
Two-meter antenna, simple (HN)		78	Aug	68
Two-meter mobile antennas		76	May	69
Vhf antenna switching without rel	р. ays	( <u>H</u> I	N)	00
K2ZSQ 10 GHz dielectric antenna (HN)	р.	<i>//,</i>	Sep	68
WA4WDL 50-MHz antenna coupler	р.	80,	Мау	75
K1RAK 50-MHz collinear beam	p	. 44	, Jul	71
K4ERO	p.	59,	Nov	69
W6DOR	p.	50,	Apr	69
50-MHz J-pole antenna K4SDY	p.	48,	Aug	6 <b>8</b>
50-MHz mobile antenna (HN) W4PSJ	p.	77,	Oct	70
144-MHz antenna, 5% wave vertica K6KLO	il D	. 40	. Jul	74
144-MHz antenna, 5%-wave vertica	Ľ, آ			
build from CB mobile whips WB4WSU	p.	67,	Jun	74
144-MHz antennas, simple WA3NFW	p.	30,	Мау	73
144-MHz antenna switch, solid-sta K2ZSO	te D.	48.	Mav	69
144-MHz collinear antenna W6R10	n	12	Mav	72
144-MHz four-element collinear ar	ray	6	May	71
144-MHz ground plane antenna, 0	.7	,	wiay	/1
W3WZA	p.	40,	Mar	69
K6HCP	p.	52,	May	70
144-MHz whip, 5/8-wave (HN) VE3DDD	p.	70,	Apr	73
432-MHz corner reflector antenna WA2FSQ	р.	24,	Nov	71
432-MHz OSCAR antenna (HN) W1JAA	р	. 58	, Jul	75
432- and 1296-MHz quad-yagi arra W3AED	iys p.	20,	May	73
Short circuit	p.	58,	Dec	73
440-MHZ collinear antenna, four-e WA6HTP	p.	ent 38,	Мау	73
1296-MHz Yagi W2CQH	р.	24.	Mav	72
1296-MHz Yagi array W3AED	р.	40	May	75
·····	μ.	,	may	

## vhf and microwave receivers and converters

Audio filter, tunable, for weak-signal communications K6HCP

communications		
кенср	p. 28, Nov	75
Cooled preamplifier for vhf-uhf	reception	
WAØRDX	p. 36, Jul	72

Fet converters for 50, 144, 220 at	٦đ			
432 MHZ W6AJF	р.	20.	Mar	68
Interdigital preamplifier and com	b-li	ne		
bandpass filter for vhf and uhf			A	70
Noise figure, sensitivity and dyna	م mic	ran	Re	70
WIDTY	;	<b>5.</b> 8,	Oct	75
Noise figure, vhf, estimating	<b>n</b>	42	lun	75
Overload problems with vhf conve	erte	rs,	Jun	/ 5
solving		53	1	70
Receiver scanner, vhf	р.	53,	Jan	73
K2LZG	p.	22,	Feb	73
Receiver, superregenerative, for v	hf	22	Int	73
Signal detection and communicat	ion	, 22	, Jui	/3
in the presence of white noise	_		<b>5</b> -6	<i>c</i> 0
Signal generator for two and six	р. met	10, ers	reb	69
WABOIK	р.	54,	Nov	69
Single-frequency conversion, vhf/ W3FOJ	uhf .ת	62.	Apr	75
Vhf converter performance,	μ.	υ,	, np.	
optimizing (HN)	_	10	11	<b>c</b> 0
Weak-signal source, stable, variab	le o	outp	ut ut	00
KEJYÖ	р.	36,	Sep	71
Weak-signal source, 144 and 432 K6JC	мн. ο.	z 58.	Mar	70
Weak-signal source, 432 and 1296	MI	٩z (		
K6RIL	p.	20,	Sep	68
WIJAA	р.	48,	Oct	75
50-MHz deluxe mosfet converter			<b>5</b> .1	
50-MHz etched-inductance bandpa	p. Iss	41, filte	rs rs	/1
and filter-preamplifiers		_		
W5KHT 50-MHz mosfet converter	5	o. 6,	Feb	71
WB2EGZ	p.	22,	Jun	68
Short circuit	p.	34,	Aug	68
WA2GCF	p.	46,	Jan	73
144-MHz converter (HN)	_	71	<b>A</b>	70
144-MHz converter, 1.5 dB noise f	p. igui	71, re	Aug	70
WA6SXC	р	. 14	, Jul	68
144-MHz converters, choosing fets	s (H n.	N) 70.	Aug	69
144-MHz deluxe mosfet converter	μ.	,		
WB2EGZ	р.	41,	Feb	71
Letter, WØLER	р. р.	71,	Oct	71
144-MHz etched-inductance bands	pass	5		
W5KHT	p	. 6,	Feb	71
144-MHz fm receiver	_	00	<b>6</b>	70
144-MHz fm receiver	р.	22,	Sep	70
WA2GBF	p.	42,	Feb	72
Added notes 144-MHz fm receiver	p.	/3	, Jui	12
WA2GCF	p	. 6,	Νον	72
144-MHz preamplifier, improved	<b>n</b>	25	Mar	72
144-MHz preamplifier, low noise	μ.	20,	in a i	
W8BBB	p.	36,	Jun	74
K6HCP	p.	72,	Oct	69
144-MHz preamp, MM5000	_	40	0-1	<b>6</b> 0
220-MHz mosfet converter	р.	49,	Uct	08
WB2EGZ	р.	28,	Jan	69
Short circuit 432-MHz converter, low-noise	P	. 76	, Jul	69
K6JC	p.	34,	Oct	70
432-MHz fet converter, low-noise WA6SXC	n	18	May	68
432-MHz fet preamp (HN)	μ.	10,	may	00
WIDTY	р.	66,	Aug	69

432 MHz preamplifier and converter
WA2GCF p. 40, Jul 75
432-MHz preamplifier, ultra low-noise
W1JAA p. 8, Mar 75
1296-MHz converter, solid state
VK4ZT p. 6, Nov 70
1296 MHz, double-balanced mixers for
WA6UAM p. 8, Jul 75
1296-MHZ noise generator
1296 MUz zroomzlifier
WAGUAM
1296.MHz preamplifier low-poise
transistor
WA2VTR p. 50. Jun 71
Added note (letter) p. 65, Jan 72
1296-MHz preamplifiers, microstripline
WA6UAM p. 12, Apr 75
1296-MHz ssb transceiver
WA6UAM p. 8, Sep 74
2304-MHz balanced mixer
WA2ZZF p. 58, Oct 75
2304-MHz converter, solid-state
KZJNG, WAZLIM, WAZVIR p. 16, Mar /2
2304-MHZ preamplifier, solid-state
2304-MHz preamplifiers parrow-band
solid-state
WA9HUV p. 6, Jul 74

## vhf and microwave transmitters

Aligning vhf transmitters				
Allen	p.	58,	Sep	68
Converting the Swan 120 to two r	net	ers o	May	69
External anode tetrodes	μ	. 0,	way	00
W6SA1	p.	23.	Jun	69
Inductively-tuned tank circuit				
W6SAI		p. 6	, Jul	70
Lighthouse tubes for uhf	_	~7		~~
Wouldv Pillpotworks caries tuned	p.	27,	Jun	69
W2FGH	<b>n</b>	42	Oct	71
Seb input source for vbf ubf tran	5V0	rtars		n'î
F8MK	р.	69.	Sep	′′70
Transistors for vhf transmitters (H	1Ň)		•	
W100P	p,	74,	Sep	69
Vhf linear, 2 kW, design data for	·		•	
WEUOV	P	. 7,	Mar	69
2C39, water cooling				
K6MYC	р.	30,	Jun	69
50-MHz customized transverter				
KIRAK	p.	12,	Mar	71
50-MHz heterodyne transmitting n	nixe	r		
K2ISP	p	. 8,	Apr	69
Correction	p.	76,	Sep	70
50-MHz kilowatt, inductively-tuned		-		
	p	. 8,	Sep	75
SU-MHZ 2 KW linear amplifier	_	16	Fab	71
50.MHz linear amplifier	р.	10,	rep	/1
KIRAK	~	38	Nov	71
50-MHz multimode transmitter	P1	00,		
K2ISP	р.	28.	Sep	70
50-MHz transmitter, solid-state				
WB2EGZ	F	o. 6,	Oct	68
50-MHz transverter				
K8DOC, K8TVP	р,	44,	Dec	68
50-MHz transverter				
WA9IGU	p	. 44,	Jul	69
50-MHz tunnel-diode phone rig				
K2ZSQ	р	. 74,	Jul	68
144-Minz Im transceiver, compact		20		~ ,
	р.	36,	Jan	14
144-WITZ TE transmitter		• •		
WOAJF	p.	. 14,	Jul	/1

144-MHz fm transmitter		_		
W9SEK 144-MHz fm transmitter, Sonobab	y F	o. 6,	Apr	72
WAØUZO Crystal deck for Sonobaby	ŗ	26, 8,	Oct	72
144-MHz heterodyne transmitting	р. mix	ers		12
K2ISP Correction	р.	), 8, 76,	Apr Sep	69 70
144-MHz linear		47	ton	60
144-MHZ linear, 2kW, design data	for	47,	Jan	03
144-MHz low-drive kilowatt linear	p	. 7,	Mar	69
W6HHN 144-MHz multimode transmitter	p	. 26	, Jul	70
K2ISP	р.	28,	Sep	70
W6AJF	p.	r 18,	Feb	70
144-MHz power amplifier, high performance				
W6UOV	p.	22,	Aug	71
W4CGC	ą	. 6,	Apr	73
144-MHz power amplifier, 10-watt solid-state (HN)				
W1DTY	p.	67,	Jan	74
Hatchett	p	. 6,	Dec	73
144-MHz transceiver, a-m K1AOB	p.	55,	Dec	71
144-MHz transmitting converter, s	olid	-sta	te ss	b 74
Short circuit	р.	62,	Dec	74
144-MHz transverter K1RAK	<b>D</b> .	24.	Feb	72
144-MHz two-kilowatt linear		26	Anr	70
144- and 432-MHz stripline amplif	ier/	trip	ler	70
K2RIW 220-MHz exciter	p	. 6,	Feb	70
WB6DJV 220-MHz power amplifier	р.	50,	Nov	71
W6UOV	p.	44,	Dec	71
WB6DJV	p.	44,	Jan	71
220-MHz rf power amplifier, fm K7JUE	p	. 6,	Sep	73
432-MHz amplifier, 2-kW W6SAL W6NLZ	D	. 6.	Sep	68
432-MHz exciter, solid-state	, ,	28	0+	60
432-MHz rf power amplifier	μ,			
432-MHz solid-state linear amplifie	p. er	40,	Apr	70
WB6QXF 432-MHz ssb converter	p.	30,	Aug	75
K6JC	р.	48,	Jan	70
432-MHz ssb, practical approach	р.	19,	Jun	70
WA2FSQ 432-MHz stripline tripler	p	. 6,	Jun	71
K2RIW 432-MHz 100-watt solid-state nowe	p	. 6,	Feb	70
amplifier	_	76	S	75
1152- to 2304-MHz power doubler	h'	50,	- ach	
WA9HUV 1296-MHz frequency tripler	p.	40,	Dec	75
K4SUM, W4API	p.	40,	Sep	69
WB6IOM	p.	6,	Aug	68
Snort circuit 1296-MHz power amplifier	р.	54,	NOV	68
W2COH, W2CCY, W2OJ, W1IMU	n.	43.	Mar	70
1296-MHz ssb transceiver	μ.			
WA6UAM 2304-MHz power amplifier	p.	. 8,	Sep	14
WA9HUV	p	. 8,	Feb	75



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Adva \_\_\_\_ 265 Aldelco \_\_\_\_ 347 Antroncraft \_\_\_\_ 381 Aptroncraft \_\_\_\_ 381 Aptroncraft \_\_\_\_ 382 Barber \_\_\_\_\_ 382 Barber \_\_\_\_\_ 383 Barry -\_\_\_\_ 382 Barber \_\_\_\_\_ 383 Barry -\_\_\_\_\_ 382 Buyers & Sellers \_\_\_\_\_ 329 Cal-Com \_\_\_\_\_ 282 Communications \_\_\_\_\_ 330 Communications \_\_\_\_\_ 330 Communications \_\_\_\_\_\_ 330 Communications \_\_\_\_\_\_\_ 330 Communications \_\_\_\_\_\_\_ 330 Communications \_\_\_\_\_\_\_ 330 Communications \_\_\_\_\_\_\_ 330 Communications \_\_\_\_\_\_\_\_ 330 Cush Craft \_\_\_\_\_\_\_ 35 D-D Ent. \_\_\_\_\_\_\_ 269 D & N \_\_\_\_\_\_\_ 269 D & N \_\_\_\_\_\_\_\_ 269 D Trake \_\_\_\_\_\_\_ 384 Danes \_\_\_\_\_\_\_\_ 324 Data Signal \_\_\_\_\_\_\_ 270 Dentron \_\_\_\_\_\_\_\_ 259 Drake \_\_\_\_\_\_\_ 385 Electronic Dist. \_\_\_\_\_\_\_ 044 Electrospace \_\_\_\_\_\_\_ 387 HR Report \_\_\_\_\_\_\_ 564 Hantronics \_\_\_\_\_\_\_ 246 Henry \_\_\_\_\_\_ 065 International \_\_\_\_\_\_\_ 056 International \_\_\_\_\_\_\_ 056 International \_\_\_\_\_\_\_\_ 333 Jan \_\_\_\_\_\_\_\_ 067 K.E. \_\_\_\_\_\_\_ 073

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NAME	
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# AdverTisers iNdex

Adver Electronic de			
Adva Electronics			101
Amtroncraft Kits Inc			175
Aptron Laboratories			113
Atlas Radio Co.			. <u>3</u> 9
Atronics			108
Barber Corporation			94
Barry			144
Bauman			111
Budwig mrg. Co.			108
Buyers & Sellers		81	. 31
CEP Communications			106
Cal-Com Systems, Inc.			112
Communications Specialist	5		2
Communication Specialties,	Inc.		112
D. R. Corbin Mfg. Co.			110
Crystal Products Co.			113
Curtis Electro Devices			110
Cush_Craft		Cove	er II
D & N Citta			103
Dames Ted			111
Data Signal, Inc.		84	85
Dentron Radio Co.		72. 73.	104
Drake Co., R. L.			1
Dycomm			68
Eimac, Div. of Varian Assoc	• • • • •	Cove	r, IV
Electropic Distributor			100
Electronic Equipment Bank	Inc		74
ELPROCON	11101		104
Electrospace Systems, Inc.			112
Erickson Communications			. 95
General Aviation			, 93
J. J. Glass Co.			65
Hat Communications Care			02
Hal-Tronix			104
Ham Radio		54 66 96	100
Hamtronics, Inc.		J4. 00, J0	102
Henry Radio Stores		Cover	r III
Hildreth Engineering			108
Hosfelt Electronics	and the second		112
Howard Micro Systems, Inc.			111
Hy-Gain Electronics Corp.			143
International Crystal Mig. (			2
lames Flectronics	, inc	88 89	109
Jan Crystals		00, 05,	76
Janel Labs			112
K-Enterprises			
			76
K. E. Electronics			76
K. E. Electronics KLM Electronics			76 112 77
K. E. Electronics KLM Electronics Kensco Communications, In Trio-Kenwood Communicatio		· · · · · · · · · · · · · · · · · · ·	76 112 77 94
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc.	nc. ns, Inc.	· · · · · · · · · · · · · · · · · · ·	76 112 77 94 31 113
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates	ic. ns. Inc.	· · · · · · · · · · · · · · · · · · ·	76 112 77 94 31 113 90
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs			76 112 77 94 31 113 90 106
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyte Products	nc. ns. Inc.	· · · · · · · · · · · · · · · · · · ·	76 112 77 94 31 113 90 106 110
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises			76 112 77 94 31 113 90 106 110 49
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Electronice Matriced Electronice	с пs, Inc.		76 112 77 94 31 113 90 106 110 49 90
K, E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics	ю. пs, Inc.	108	76 112 77 94 31 113 90 106 110 49 90 59
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electro	nc, ns, Inc.	108,	76 112 77 94 31 113 90 106 110 49 59 109
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electro Northshore RF Technology	nc, ns, Inc.	108.	76 112 77 94 31 113 90 106 110 49 90 59 109 104 110
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Lyle Products MFJ Enterprises Maynard Electronics M-Tech New England Digital Electro New England Digital Electro	nc. ns, Inc.	108,	76 112 77 94 31 113 90 106 110 49 90 59 109 104 110 113
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electrr Northshore RF Technology PRA Industries Dece	ns, Inc.	108,	76 112 77 94 31 113 90 106 110 49 90 59 109 104 110 113 103
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matrics Mariard Electronics M-Tech New England Digital Electrr Northshore RF Technology Pagel Dagung Congineers	c. ns, Inc. pnics	108,	76 112 77 94 31 100 100 100 109 109 109 104 110 113 103 111
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communication Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Marine Maynard Electronics M-Tech New England Digital Electro New England Digital E	onics	108,	76 112 77 94 31 100 100 100 100 100 100 100 100 100
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electro Northshore RF Technology PRA Industries Pagel Palomar Engineers Poly Paks Porta-Pak R F Communications	ic. ns. Inc.	108. 82.	76 112 77 91 113 90 106 110 49 90 104 100 113 103 111 103 111 90 104 103 104 103 103 112 80 104 103 104 103 112 106 106 106 106 106 106 106 106 106 106
K. E. Electronics. KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Maric MFJ Enterprises Maric Maynard Electronics M-Tech New England Digital Electro New England Digital Electro	onics	108,	76 112 77 94 113 90 106 110 49 90 50 109 109 109 109 109 103 111 98 86 90
K. E. Electronics. KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electro Northshore RF Technology PRA Industries Pagel Palomar Engineers Poly Paks Porta-Pak R F Communications RMS Corporation RP Electronics	ic.	108,	76 112 77 94 31 113 90 106 110 59 109 109 104 110 103 103 111 98 110 866 8068
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Maric Maynard Electronics Maynard Electronics Maynard Electronics New England Digital Electro New England PAI Industries Pagel Palomar Engineers Porta-Pak R F Communications RMS Corporation RP Electronics Radio Amateur Callbook	nc. ns, Inc.	108, 82, 69,	76 112 77 94 31 113 90 106 110 59 109 109 109 109 109 109 109 100 113 113 90 68 82
K. E. Electronics. KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electro Northshore RF Technology PRA Industries Pagel Palomar Engineers Poly Paks Porta-Paks Porta-Paks RF Communications RM Corporation RP Electronics Inc.	ponics	108, 82, 69,	762 1122 777 94 31 113 900 100 49 900 100 100 100 100 100 110 110 100 10
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matrics Marrier New England Digital Electrr Northshore RF Technology Page Industries Pagel Palomar Engineers Poly Paks Porta Paks Porta Paks Ref Communications RF Comporation RP Electronics Radio Amateur Callbook Regency Electronics, Inc. Sa Electronics	inc.	108, 82, 69,	762 1122 777 94 31 1133 900 106 1100 109 109 109 109 109 109 109 109 10
K. E. Electronics. KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MATric Maynard Electronics MTech New England Digital Electro Northshore RT Fechnology PRA Industries Pagel Palomar Engineers Poly Paks Porta-Paks Porta-Paks RF Communications RM Corporation RP Electronics Seguel Electronics, Inc. Seguel Electronics	nc. ns, Inc.	108, 82, 69,	762 94 31 1139 1066 1109 900 59 109 104 1103 113 1103 1113 1103 1113 1103 1113 1103 1105 68 82 63 1100 105
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electrn Northshore RF Technology PRA Industries Pagel Palomar Engineers Poly Pak Porta-Pak R F Communications RMS Corporation RP Electronics Radio Amateur Callbook Regency Electronics, Inc. SSagal Electronics Sagal Electronics	c	108, 82, 69,	766 1122 77 94 31 113 90 106 49 959 109 109 109 109 109 109 109 88 82 63 110 88 82 63 110 68 82 63 110 68 82 63 110 68 82 63 110 68 82 63 110 68 82 63 110 82 63 110 68 82 63 110 68 82 63 110 68 82 63 110 68 82 63 110 68 82 63 110 68 82 63 110 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 106 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 100 80 80 100 80 80 80 100 80 80 80 100 80 80 80 80 80 80 80 80 80 80 80 80 8
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Marinar Electronics M-Tech New England Digital Electro New England Digital Electro Regel Paks Porta-Pak R F Communications R F Communications R F Electronics Sagal Electronics Sagal Electronics Saroc Savoy Signal Management Science	sources	108, 82, 69,	766 1122 77 94 31 106 110 90 59 109 109 59 109 109 109 109 109 109 109 109 109 10
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics MTech New England Digital Electro Northshore RF Technology PRA Industries Pagel Palomar Engineers Poly Paks Porta-Paks Porta-Paks RF Communications RMS Corporation RP Electronics Radio Amateur Callbook Regency Electronics, Inc. SSat Electronics SAROC Savoy Signal Management Science	C	108,	767 1122 77 94 31 113 90 106 110 49 90 109 109 109 109 109 109 109 109 109
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matrics Mariard Electronics M-Tech New England Digital Electro Northshore RF Technology Page Industries Pagel Palomar Engineers Poly Paks Porta-Paks Porta-Paks Parta Paks Parta Paks Pateronics Constant Refectornics Sal Electronics Sal Electronics Sal Electronics Sal Electronics Sal Electronics Sal Management Science Signal Management Science Southwest Technical roduc	c	82.	76 112 77 94 31 100 100 90 90 100 100 100 100 100 100
K. E. Electronics. KLM Electronics S. Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electro Northshore RF Technology PRA Industries Pagel Palomar Engineers Poly Paks Porta-Paks Porta-Paks Porta-Paks Porta-Paks Porta-Paks RF Communications RMS Corporation RP Electronics Sagal Electronics Sagal Electronics Sagal Electronics Sagal Electronics Sagal Electronics Sagal Electronics Sagal Electronics Co. Southwest Technical Produc Space Electronics Produce Southwest Technical Produce Space Electronics Produce Sagate Electronics Co.	C	108, 82, 69,	76 1127 94 31 113 906 109 909 109 1004 1100 1004 1100 1005 822 1100 88 82 31100 105 82 1100 105 82 1100 105 82 1100 105 105 105 105 105 105 105 105 10
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Asociates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electrn Northshore RF Technology PRA Industries Pagel Palomar Engineers Poly Pak Porta-Pak R F Communications RMS Corporation RP Electronics Sagal Electronics Sagal Electronics Sagal Electronics Sagal Electronics Savoy Signal Management Science Subwest Technolog Produces Southwest Technolog Produces Specialty Communications 1 Specialty Communications	c ns, Inc. onics S S S S S S S S S S S S S S S S S S S	108, 69, 67	76 1127 94 31 113 90 100 49 959 109 109 109 109 109 109 109 109 109 10
K. E. Electronics. KLM Electronics S. Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MATric Maynard Electronics M-Tech New England Digital Electron Northshore RF Technology PRA Industries Pagel Palomar Engineers Poly Paks Porta-Paks Porta-Paks Porta-Paks Porta-Paks Porta-Paks RF Communications RMS Corporation RP Electronics Sagel Electronics Sagel Electronics Sagel Electronics Sagel Electronics Sagel Electronics Corp. Southwest Technical Produc Specialty Communications Spectronics, FM Spectronics, FM	c	108, 82, 69, 87,	767 1127 944 113 900 1000 499 909 1004 1001 113 103 1005 1005 1005 1005 1005 1
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electro Northshore RF Technology PRA Industries Pagel Palomar Engineers Poly Paks Porta-Pak R F Communications RMS Corporation RP Electronics Radio Amateur Callbook Regency Electronics, Inc. SST Electronics SAROC Savoy Signal Management Science Southwest Technical Produc Spectary Communications Spectrum International Syan Electronics	s system:	108, 82, 69,	76794 1127794 3113906 11099599 1099599 1099599 1004990 110522 10052 100522 100520
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products Matrier Matrier Balomar Electronics Matrier New England Digital Electron New England Digital Electron Varthshore RF Technology PRA Industries Pagel Palomar Engineers Porta-Pak Porta-Pak R F Communications RF Corporation RF Electronics Sagal Electronics Sagal Electronics Sagal Management Science Signal Management Science Signal Management Science Signal Management Science Spectronics, FM Spectronics Spectronics Inc. Spectally Communications S Spectronics, FM Spectronics Spectronics Spectronics Spectronics Spectronics Co. Spectally Communications S Spectronics FM Spectronics Spectronics Spectronics Spectronics Spectronics FM	c. ris, linc.	108, 69, 87,	767 1127 944 113 906104 109 599104 10959104 10959104 1007 1007 1007 1007 1007 1007 1007 1
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics M-Tech New England Digital Electro Northshore RF Technology PRA Industries Pagel Palomar Engineers Poly Paks Porta-Pak R F Communications RMS Corporation RP Electronics Radio Amateur Callbook Regency Electronics Sagal Electronics Sagal Electronics Sagal Electronics Sagal Electronics Sagal Electronics Communications Sagal Electronics Sagal Electronics Cop Southwest Technical Produc Spacetally Communications Spectrum International Swan Electronics Systems Research, Inc. Ten-Tec Electronics	G. Ins. Inc. Ins. Inc. Systems	108, 82, 69,	767 1127 944 113 906 1100 499 599 104 1103 1103 1103 1103 1103 1103 1103
K. E. Electronics KLM Electronics Kensco Communications, Ir Trio-Kenwood Communicatio Kolar, Inc. Levy Associates Little Giant Antenna Labs Lyle Products MFJ Enterprises Matric Maynard Electronics MFJ Enterprises Matric Maynard Electronics Pagel Paiomar Engineers Poly Paka Poly Paka Corporation RP Electronics Radio Amateur Callbook Regency Electronics, Inc. SST Electronics SAROC Savoy Signal Management Science Silep Electronics Co. Southwest Technical Produc Spectaur International Systems Research, Inc. Ten-Fector Corporation Systems Research, Inc. Ten-Fector Corporation Toutec Corporation	s s s	108, 69, 87,	767944 11277944 113060 11007999 1004999910 10059910 10059910 10059910 10059910 10059910 1005900 1005900 1005900 100500000 1005000 1005000 1005000 1005000 10050000 10050000 10050000 10050000 100500000000
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