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HISTORY

Marconi's first experiments

POTLIGHT

The perfect micropower op amp?

REVIEW

PC based speaker testing

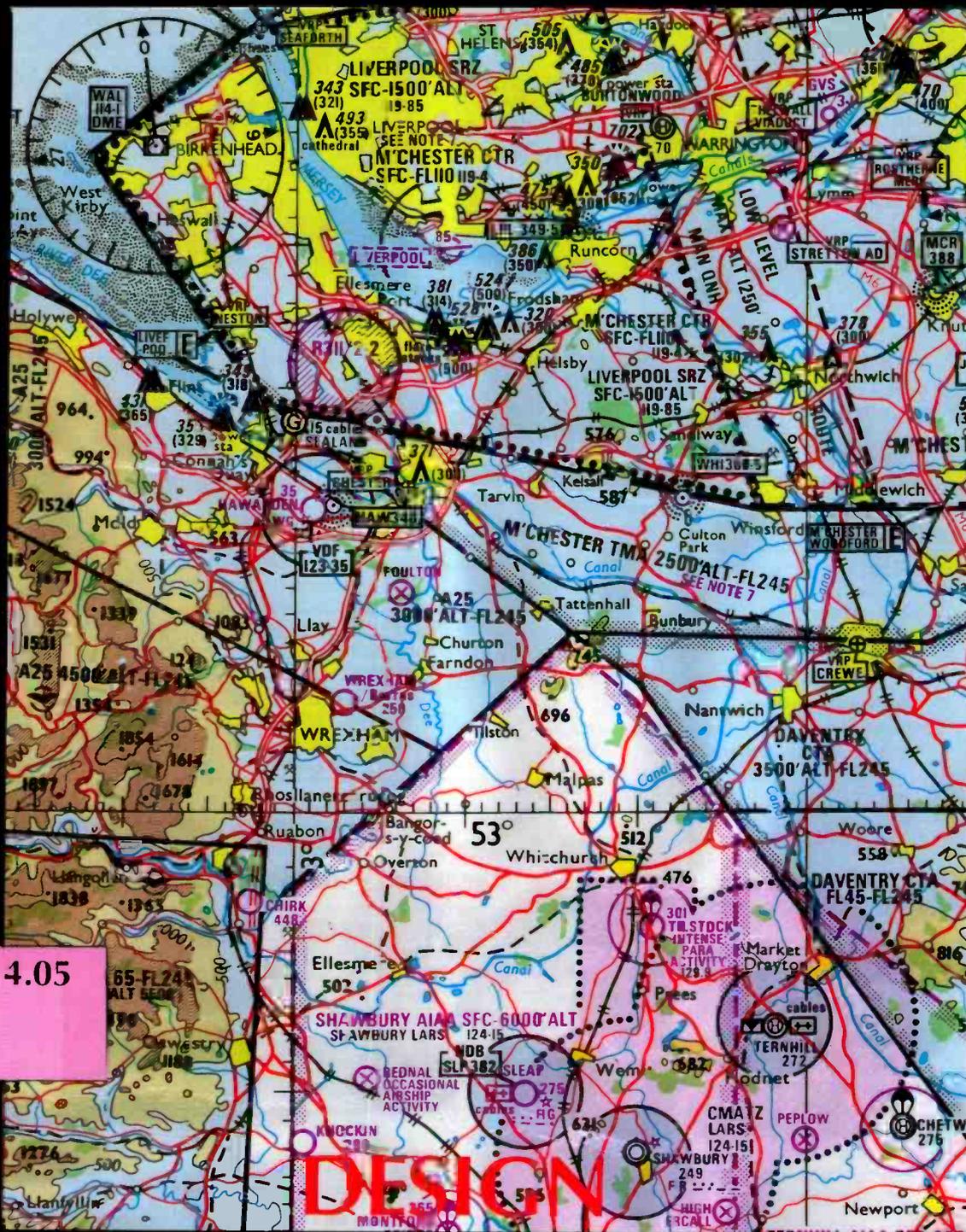
SIMULATION

Working with PSpice

FREE SOFTWARE* PSpice 4.05

Zetex transistor models

circulation only. See p6 for details.



Electronic fluxgate compass



Omni-Pro II - The Next Generation

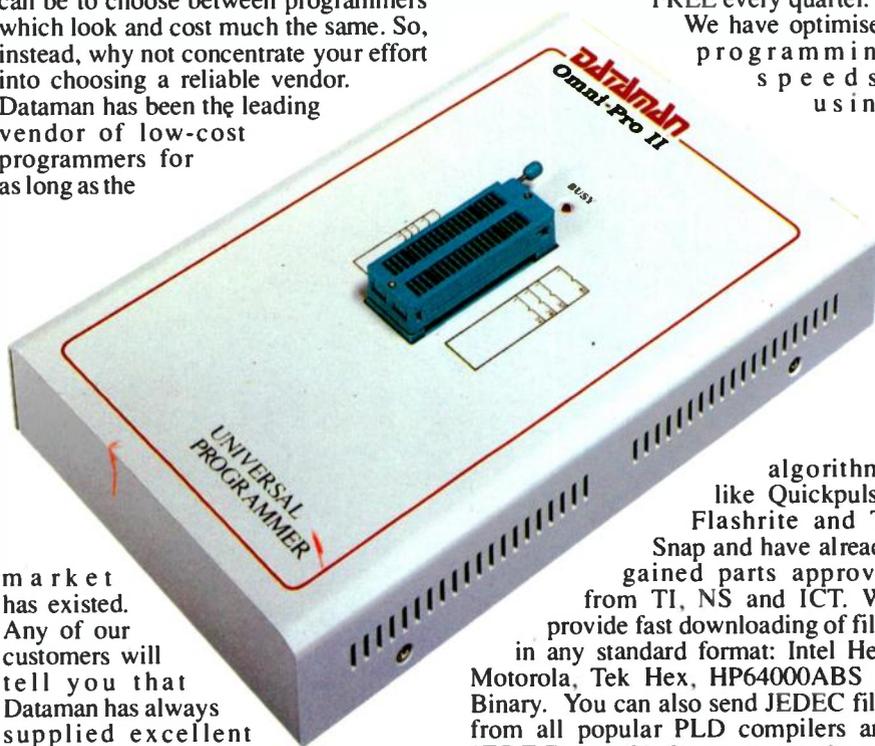
When you get a new product, what are your main concerns? Freedom from frustration is certainly one important consideration, for your time is valuable. You will want a product which is reliable and sophisticated, yet simple to use, with clearly written documentation. You will be looking for a high standard of technical support and regular upgrades for the product.

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Truly Universal

Omni-Pro II has universal pin-drivers which will accommodate a very wide selection of parts. You can program BIPOLARS, PROMS, E/EEPROMS, PALS, GALS, FPLAS, PEELS, E/EEPROMS and MICRO-CONTROLLERS. The latest FLASH EPROMS are supported too. The list has 1250 devices already and substantial numbers of new devices will be added FREE every quarter.

We have optimised programming speeds, using



market has existed. Any of our customers will tell you that Dataman has always supplied excellent well-supported products. That's why we're still here! We take technical support seriously. We give you your money back, if you're not satisfied. These are important points to consider. But now let's take a look at some of the special benefits of owning Omni-Pro II.

What Benefits?

Well, for instance, the interface is not via the computer's parallel port, which is speed-limited, and probably connected to your printer. A dedicated plug-in half card performs fast data transfers.

The software is a professional package in full colour that will run in only 400K of RAM. What's more it will run on any PC/AT or compatible - even the latest 486 machines. That's because Omni-Pro II has its own independent clock - some programmers rely on the computer for timing, and won't work with faster machines.

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Omni-Pro II - complete £495

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In next months issue: Receiving teletext on the PC. Laurence Cook describes in detail the hardware/software mix to download teletext pages onto a PC. The age of the electronic newspaper has arrived.

FREE PSPICE V4.05
software +
Zetex transistor models
See p6 for details...

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24 PIN PRINTER

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Raising the national interest

As I sit here writing this the Maastricht summit approaches. By the time this gets read, the meeting of European heads of state will be largely forgotten. But there are some things which deeply affect industries dependent on long term investment, particularly electronics.

The Government tells us that we must not lose control of our currency, that economic and monetary union would place a straightjacket on the UK treasury, that we would no longer be in control of our own destiny. For instance, the Government expresses concern that subjugation to a European treasury would restrict its freedom to use interest rates as an instrument of economic control.

I submit that the Government has already relinquished control of UK monetary policies, a factual observation without any particular political bias. Mrs Thatcher came into office determined to free the UK from the strictures of a command economy, the notorious stop-go policies of previous conservative and labour chancellors alike. Her crystal clear view of the world determined that everything would find its own level and purpose if it could be freed from the dead hand of bureaucratic control.

She applied this to the economy with a vengeance. In 1981, the Treasury lifted all foreign exchange controls. International Money could come and go as it pleased. It could walk across national borders, it could dictate its own terms to the helpless local development authorities crying out for inwards investment, it could play whole countries off against each other for its favour.

Most countries responded with visible and invisible barriers. For instance the French telecommunications industry put together a careful procurement policy which effectively ruled out the purchase of anything which wasn't designed and built in France. The Japanese hid their industries

behind impenetrable local standards for imported goods while at the same time orchestrating their outward investments to largely exclude leading technology transfer.

The freewheeling Reaganomics of the US in the eighties embodied much of Mrs Thatcher's vision of a totally free market. Its application very nearly killed the US semiconductor industry. It actually succeeded in the destruction of a US owned consumer manufacturing base.

The relaxation of credit controls has been equally damaging to the UK; when International Money packs its bags to live overseas, the Treasury can do no more than rack up the interest rates to entice it back. For instance, an engineering company needing cash for investment has to guarantee returns to International Money which match those on offer from the Treasury – why should Money spend its time on short term holiday in the electronics industry when it can get a better return from the banks? Although interest rates have come down some four points since their peak, they are still around eight points above the inflation rate, an historic high.

Mrs Thatcher's vision of a deregulated economy has placed our national industries in direct competition with the Treasury for investment funds, a truly extraordinary situation. After all, it would seem logical that our companies should compete against their foreign counterparts rather than the banks.

The loss of money controls with the exception of the interest rate is the same problem which has successively bedeviled chancellors Howe, Lawson, Major and Lamont. Going for a single euro-currency is simply recognition that a UK chancellor is now powerless.

Why not hand over the keys of office to Brussels? It currently stands more chance than we do of bringing International Money to heel. **Frank Ogden.**

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REGULARS

UPDATE

Spacecraft antenna put to the test

Queen Mary & Westfield College, part of the University of London, has opened a millimetre-wave compact antenna test range (CATR) allowing radiation characteristics of spacecraft antennas to be measured at frequencies up to 200GHz in a clean room environment.

The facility will allow RF testing of AMSU-B (advanced microwave sounding unit), a satellite-borne microwave radiometer funded by the UK Meteorological Office. The instrument is being developed by British Aerospace to fly on future NOAA series weather satellites and the European and US Polar platforms.

Funding for the laboratory has been provided mainly by the UK Science & Engineering Research Council (Serc) under a rolling grant system.

The CATR consists of special reflector panels, a custom-built transparent tenting and air conditioning system, and a rail-mounted positioning system and turntable – all housed in an anechoic chamber.

Computer controlled test and measurement equipment includes an HP 9000 model 310 desk-top computer and a 375 Unix workstation connected to an Ethernet lan for pattern processing and file transfer.

PC on a chip

A single chip ms-dos computer is now a bit nearer with the release of a single device which integrates an 80C86 processor, systems logic, CGA graphics and a serial port.

Produced by US semiconductor company Chips and Technologies, the 8680 also features power management, memory controller and device emulation capabilities within a low cost 160 pin VLSI package.

The CPU has the complete instruction set of the 80C86 together with a few new ones to extend the operating environment. The fully static device runs up to 14MHz, realising three mips performance.



CATR control room at Queen Mary & Westfield College overlooking the range's test chamber.

Eastern Europe open

The fall of the Berlin wall and the opening up of Eastern Europe to Western style capitalism is prompting a number of initiatives and potential big money contracts for western companies. But the unsteady political climate is still hitting military expenditure.

In Britain, the Royal Society is pushing for closer scientific relationships between the UK and the USSR and other Eastern Bloc countries by encouraging young postdoctoral scientists from those countries to make visits to the UK to acquire new scientific skills.

It has already signed agreements with Hungary, Poland and Czechoslovakia which will allow 12 postdoctoral fellowships from each country to be made available annually for visits to the UK.

Support for the Hungarian programme has been provided by the Foreign and Commonwealth Office (FCO) and the Soros Foundation and the first 12 fellows have come to the UK.

The Royal Society has also received a grant from the Wolfson Foundation plus extra support from the FCO to start the Polish and Czechoslovakian programmes.

A separate programme for the USSR has been developed with financial support from the FCO and the Society's Parliamentary Grant-in-aid.

In the US, the National Association of Broadcasters (NAB) is trying to establish sister station agreements between broadcast stations in the US and USSR. The initiative will involve the support of the US Information Agency which is responsible for the Voice of America.

Edward Fritts, NAB president, says the programme's objective will be to strengthen the cultural, educational, economic, and professional ties between participating US and USSR stations.

Cable & Wireless has signed its first joint venture agreement with Russian partner Comincom to establish and operate digital overlay networks in Nakhodka and Sakhalin in eastern Russia.

These will use international telephone, fax and data communications from C&W subsidiary Hong Kong Telecom. Each network will use 34Mbit/s microwave links interconnecting the earth stations and exchanges. Initially radio links will connect customers in Nakhodka and cable

UK particle detector for US

An advanced particle detector, designed and built at the Science and Engineering Research Council's Rutherford Appleton Laboratory is ready for shipment to the Stanford Linear Accelerator Centre. When installed in the accelerator it will detect and measure particles containing charm and beauty quarks from high energy reactions at the SLAC Linear Collider.

Quarks decay rapidly – lasting only about a million millionth of a second. To detect these particles and record their very short flight paths prior to decay, the design incorporates 480 charge coupled devices in a mosaic. Each CCD consists of a matrix of charge storage elements; in all there are 120million. This is the first time that so many CCDs have been used together in a single detector, giving a unique tracking precision of 0.005mm



Emergency call: Police forces have been turning to electronics to improve their response to emergencies. For example, a version of Walton Radar Systems' air traffic control digital voice recorder, Hindsight-DVR, can be used to allow 999 distress calls to be replayed rapidly allowing crash sites to be identified with pin-point accuracy within minutes of an incident. Avon & Somerset constabulary is having a Racal-Datcom data and voice communications network installed across 56 police stations in the area. Another division of the firm, Racal Recorders, is installing its Callmaster voice processing system at Hampshire Police headquarters in Winchester. The force is only the second customer for Callmaster; the first was Tomy Toys.

Betacam boost

There's still life in the old video dog. Broadcast Television Systems (BTS) is sticking with the Betacam format for professional post-production applications and is joining with Sony in developing digital Betacam, a 0.5in components digital video recorder suitable for the 625/50 market.

The recorder, planned for 1993, will be able to play analogue and digital Betacam SP recordings. BTS plan to push for this format to become a worldwide production standard.

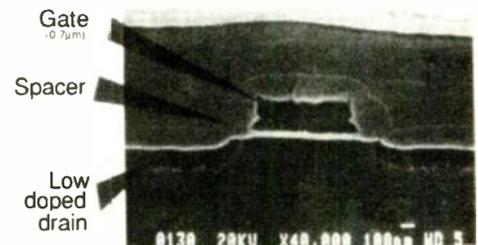
Pieter van Dalen, BTS president, says that because Betacam has proven itself to be a durable tape standard over the last ten years, BTS believes it is the best solution for the multiple needs of this industry.

Joint venture for 0.7µm asic design

A 0.7µm cmos asic manufacturing process has been developed as part of the Jessi Logic and Esprit Acces projects. Several million ecu of investment have been committed for a new wafer stepper, metal sputters and etchers.

Until now 0.7µm has only been available internally in semiconductor companies where the production of a new standard part, such as a dram, will typically involve adjustments to the fabrication process and equipment to improve yields. This is not suitable for asic customers who need a stable process with short turnaround times.

The new process, called ECPD07, was jointly developed by ES2 and Philips and has already been installed by ES2 where, compared with the firm's existing 1µm process, it results in an area shrinkage to 64% from a previous size; speed improvement is 50%.



The ECPD07 0.7µm process resulted from a joint venture

for business - sometimes

distribution links in Sakhalin.

Lord Young of Graffham, C&W's executive chair, says: "We have worked with Comincom and our other Russian partners throughout the recent developments in Russia. We are aware that these two joint ventures are just a start."

Comincom was established to build up and operate separate digital overlay networks in the USSR and its main activities are to provide commercial international telecommunications services and establish and operate international telecommunications centres and local networks to connect customers to them.

A Kozhanov, director general of Comincom, said he thought that such projects "will make our countries still more friendly and help Russia become closer to the world community."

Military upset

These closer links have, not surprisingly, hit into military budgets and have upset a number of western companies. The attitudes of these countries were summed up by a recent report from market watchers Frost & Sullivan.

The report commented: "Although democracy's return to fashion has turned the tide in terms of European security, it has prompted many politicians to make defence cuts instead of recognising that changes such as these require more defence rather than less."

This followed the research group's prediction that the European market for military electro-optic products is forecast to grow only marginally from US\$1.17 billion in 1991 to US\$1.35 billion by the end of 1996.

The report goes on to say that "military electro-optics are, for the most part, a highly defensive activity, and so Europe could spend a great deal more on electro-optic systems without breaking treaties or inviting aggression. It is self-justifying in that an electro-optic technique generally calls for development of a counter measure, and a counter measure requires development of a new electro-optic technique, and so on."

With attitudes such as these, it is clear to see why the military merry-go-round goes on, perhaps more slowly, but not as yet in reverse.

Writing on the wall for domestic teletext?

The government's sale of teletext capacity on the commercial TV channels to big business is coming under heavy criticism for robbing the existing public service of 40% of its capacity.

The move has been made by the Home Office to increase the capacity available for commercial services sixfold. Capacity will now be sold off to the highest acceptable bidders, with the cash payable to the Treasury. Critics point out that money from the sale goes straight to the government, but the seven million people who have already bought teletext sets, and are buying at a rate of 0.1 million a month, will get a reduced service after the end of next year.

Behind the scenes the Independent Television Commission has fought hard to protect consumers who could have lost the entire service.

In fact the business capacity generated by the public cuts is so large that the ITC has had to split it into three packages for auction. National Transcommunications Ltd, recently sold by the Home Office to Mercury Asset Management, wins too, because NTL has a monopoly on carrying commercial services until 1996. The general public will have no access to these new services because they will be encrypted with decoders available only to closed user groups.

The ITC is also auctioning off the public service – to the highest bidder – with the Treasury getting the money. But the capacity for this service is so reduced that the ITC will offer only one franchise, with capacity spread over the two channels, ITV (soon to be called Channel 3) and Channel 4.

Although the consumer issues are clouded by a tangle of complicated technical facts and difficult comparisons, the 40% cut in public teletext capacity means a clear loss to the viewer. Viewers will either find fewer pages of text information from which to choose; or will have to switch channels to find them. Or it will take longer for selected pages to appear on screen. The only way viewers will be able to compensate for the

capacity loss is to buy a new TV set which contains a large digital memory capable of storing pages in anticipation of use. These sets will be far more expensive than conventional sets.

The European teletext system slots digital data, running at a speed of around 7MHz, into the spare picture lines, or vertical blanking interval, which make up the black borders at the top and bottom of the screen.



Teletext TV sets decode and display this data as pages of information.

There are 25 VBI lines, but the maximum number available for teletext, without risk of interference to non-teletext TV sets, is 12. Currently Channel 4 uses all 12 whereas ITV sells off one line for commercial closed group business services. Two years ago the Home Office proposed that all the available lines should be auctioned off to the highest bidder, either private or commercial. The Independent Broadcasting Authority, now the ITC, feared that the highest bidders would be business users and there would be no public teletext on commercial TV. The IBA and ITC pushed the Home Office to a guarantee of 6 lines for public teletext and then 7.5 lines.

The ITC will now grant just one licence to run for ten years from January 1 1993. This

will cover both ITV/Channel 3 and Channel 4. Although the single licence creates a pool of 15 lines, viewers will have to switch channels if the service operator puts different text information on each channel.

ITC describes this as a 30% reduction, but the figure is misleading because it is based on the situation in the spring, when broadcasters were using fewer lines. The real reduction, from 12 to 7.5, is nearly 40%.

Putting on a brave official face, the ITC reassures viewers that future technical developments will give the appearance of faster access from fewer lines – enabling technology is extra memory in the TV set.

Each page of text needs 1Kbyte. Most teletext sets have only a one page store. If extra kilobytes of memory are added, the receiver can store extra pages in anticipation of selection. But as the TV set has no way of knowing what pages the viewer will select, this is a hit and miss approach.

The ultimate solution – enough memory to store all pages – is prohibitively expensive.

Manufacturers already add around £70 to the price of a TV set for a decoder and single page store which costs less than £5 to fit.

By restricting public teletext, the government has released three lines per channel for commercial services. Under the Broadcasting Act 1990, these can be used for closed user group business information, such as chain-store stock control and banking transactions. This gives a total of six lines, a six-fold increase on the current business capacity.

The ITC has split these into three franchises. One will get two lines on Channel 3, another will get two lines on Channel 4 and the third will get one line each on Channels 3 and 4. The auction has begun, without public consultation. Fourteen businesses have already expressed interest in bidding.

Barry Fox

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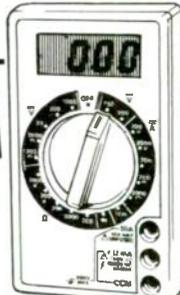
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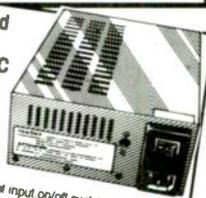
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RESEARCH NOTES

High power laser lenses – not just a mirage?

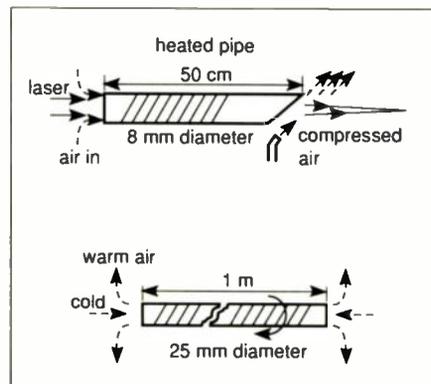
Why is the respected science magazine *Nature* (Vol 353, No 6344) carrying on its front cover a hazy picture of a water tower looking as though it were taken with either a pinhole camera or some battered old box brownie? The remarkable answer is that the 5km-distant tower was photographed through a lens consisting of nothing more than heated air!

Max Michaelis of the University of Natal in South Africa, who took the photograph, explains that the idea of exploiting the change of refractive index with temperature is far from new. Bell Labs experimented with gas lenses for focusing laser beams

way back in the 1960s, but found difficulty in overcoming the effects of air turbulence on the image sharpness.

The basic gas lens consists of a heated pipe through which air is passed. The air nearest the pipe wall becomes hotter than that flowing down the middle and as a result has a lower refractive index. The whole aperture of the pipe thus behaves like a lens – or as Max Michaelis describes it – a “rolled up mirage”.

What Michaelis and his colleagues (Drs Cunningham, Notcutt, Waltham and research workers Prause and Dempers) have now published are details of a relatively



Top, Air passes through a heated pipe so that air nearest the pipe wall becomes hotter than that near the middle, has a lower refractive index and so produces a “rolled up mirage”.

Bottom, Spinning the tube looks to overcome the problems of asymmetry caused by gravity and turbulence.

Shock, horror model probe

How shocking are you? Researchers at Sandia National Laboratories in Albuquerque, New Mexico, could give you the startling truth using a simulator they have developed to mimic the severe static electric discharge that can be triggered by a human body.

The severe human body electrostatic discharge tester (SSET), was designed to test devices and electronic systems which can malfunction or be destroyed if subjected to such a shock. Static electricity is an accumulation of charge on an insulated object and can be produced when a person walks across a carpeted floor, gets out of a car or even stands outdoors in the wind. When this accumulated charge is suddenly transferred to another object or person, either through direct contact or a spark, the electrostatic discharge (ESD) can be unpleasant, to say the least.

But more than just causing annoying electric shocks, ESD can result in significant losses in terms of life and property. In the US electronics industry, losses associated with ESD are estimated at between \$0.5 and \$5bn annually. Unintentional detonation of explosives (fireworks, industrial explosives, etc) is also an obvious danger.

When human beings acquire charge, the potential difference between the body and the ground will normally rise to between 6 and 12kV. But under dry conditions (10 to 20%

relative humidity), a person can develop and sustain voltages of about 35kV. Normally it is difficult to sustain voltages of greater than 25kV due to the corona effect where some of the accumulated charge disperses.

Sandia researchers have investigated factors influencing ESD effects such as maximum sustainable voltages, humidity and individual height. A database assembled from scientific literature concerning measurements of human body electrical parameters (voltage, capacitance, resistance and inductance) has been developed into an electrical model of the human body.

The model uses extremes of documented data to define a severe human body ESD for use in qualification testing of systems with stringent safety or reliability requirements. It exhibits the distinctive characteristics of an actual human body ESD waveform, having an extremely fast rise time to peak current (approximately 1ns), and an initial voltage of 25kV. It also specifies that current be injected directly into a test object without a spark, replicating the most severe stress created by an ESD.

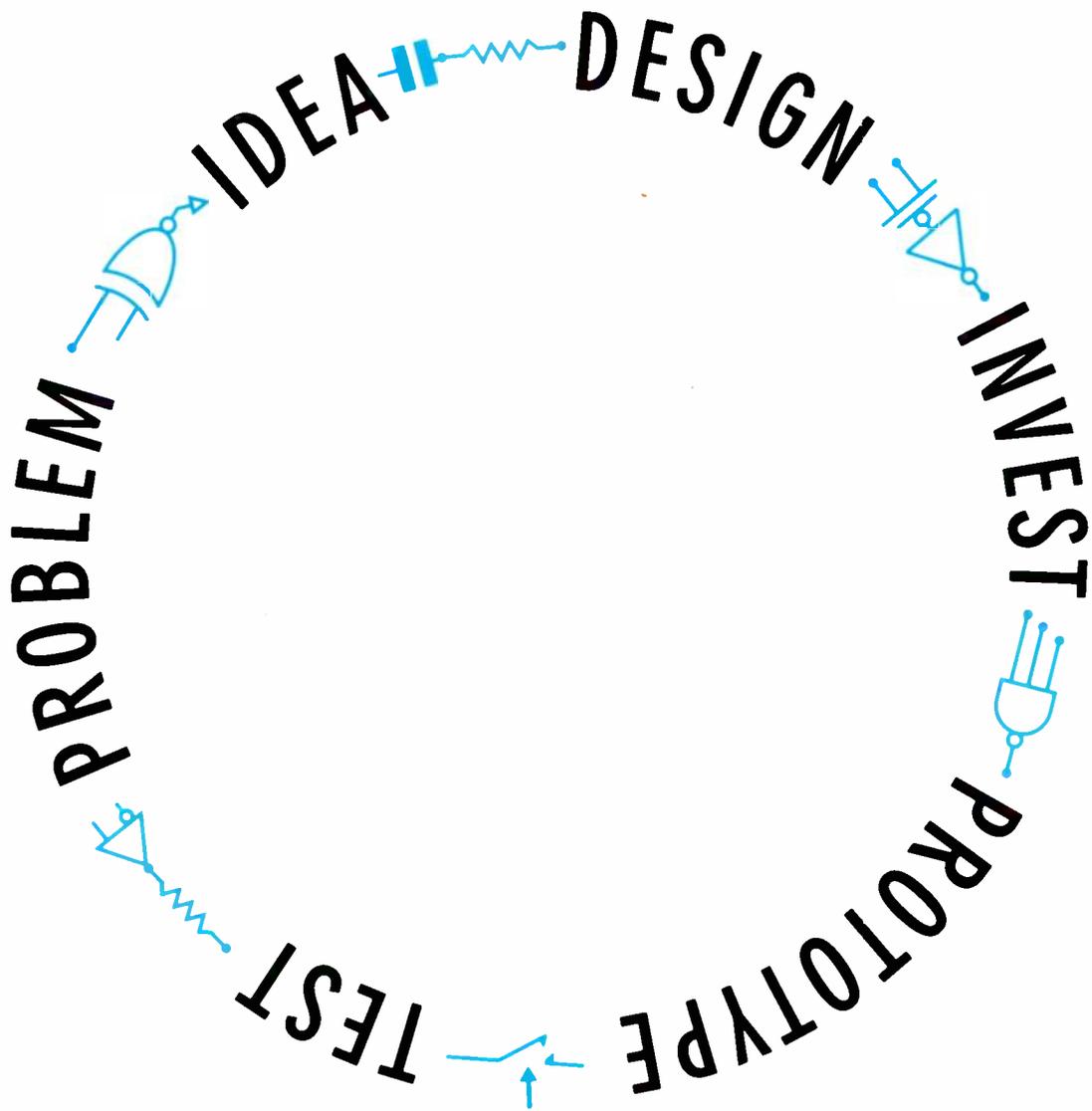
The model has been used to develop the SSET, a practical discharge tester which is constructed from off-the-shelf components costing approximately \$750 excluding the power supply. Objects to be tested are attached directly to the coaxial output of the SSET.

simple way of overcoming the problems of asymmetry caused by gravity and turbulence. The solution is to spin the tube at 30Hz, allowing creation of reasonably good lenses of up to 5cm diameter – much larger than the 8mm stationary gas lenses.

But why go to all this trouble when you can make a far more accurate lens from a few pence worth of glass or plastic? The answer is that gas lenses are virtually indestructible and can tolerate optical power levels that would vaporise a glass lens almost instantly.

Michaelis and his group have used gas lenses to focus carbon dioxide laser beams to drill holes in 1mm sheet steel. They also point to the prospects of using highly focused laser beams for

Continued over page



Break the circuit

A product can always benefit from being smaller, faster, cheaper or simply more efficient.

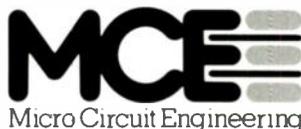
But the route to these improvements is often through new technology.

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Gas telescope image of a water tower at a distance of 5km..

satellite propulsion. Such beams could be used either to nudge satellites already in orbit or even to help place them in orbit. Suggestions have long been around for lifting a satellite to about 10km by balloon and then raising it further with a laser beam. No conventional lens or mirror could handle anything like the required power.

In their paper, Michaelis *et al* say the damage threshold intensity for short optical pulses through glass or germanium lenses is around 1GW/cm². Gas lenses, by comparison, can handle intensities a hundred times greater.

For a more down-to-earth application of gas lenses, there is the prospect of laser-induced fusion power. Such lenses could focus the very powerful lasers needed to make atoms of hydrogen fuse together and release their energy. Michaelis says that the pulses required for the process are equivalent to about a tonne of TNT, adding

with some mild understatement, that a tonne of TNT would do an awful lot of damage to glass components.

Beyond these rather awe-inspiring applications, there are also simpler gas lenses that can be made by exploiting the difference in refractive index between any gas and a vacuum. Quite recently it has been suggested that the problems of the ill-fated Hubble space telescope could be solved by using a transparent bag of helium as a sort of giant contact lens!

Max Michaelis is confident that, though few people take seriously the idea of all-gas telescopes in space, the whole subject is still very much in its infancy. Given more research, gas lenses could one day out-perform solid lens or mirrors. They would have very low transmission losses and would not suffer from distortions arising from their mass. Perhaps one day we will see the all-inflatable space telescope ...propelled cheaply into orbit by gas-focused laser?

Sunk without a trace... of radioactivity

A few years before the birth of Christ, a not-very remarkable event took place. A Roman freighter of the class *navis oneraria* sank off the coast of Sardinia carrying a heavy cargo of lead. Around 1500 hand-marked ingots weighing a total of 50t were probably on their way to some ancient building site, to be made into water pipes or stone clamps. Since that rather unmemorable incident all the ingots have lain untouched in about 30m of water – until now when they have become the subject of excited interest to modern physicists.

The reason, or part of it, is that the cargo has been largely shielded from contamination. So this special ancient lead is extremely low in radioactivity. Modern lead, by contrast, is almost universally contaminated with minute traces of radioactive lead-210, bismuth-210 and polonium-210.

For most normal purposes such contamination is so insignificant that it can be ignored; but not when it comes to shielding detectors searching for the radioactive signatures of rare natural processes such as the interactions of solar neutrinos.

Discovery of this cargo led to an interesting collaboration earlier this year between physicists at the Instituto Nazionale

di Fisica Nucleare (INFN) and archaeologists representing the Italian authorities for artistic and historic heritage. According to a report (Cern Courier, Vol 31, No 7), this collaboration will give INFN access to a priceless material for use in the underground Gran Sasso Laboratory in exchange for support for the archaeologists in setting up a database of all the recovered artefacts.



Photo: Cern Photo

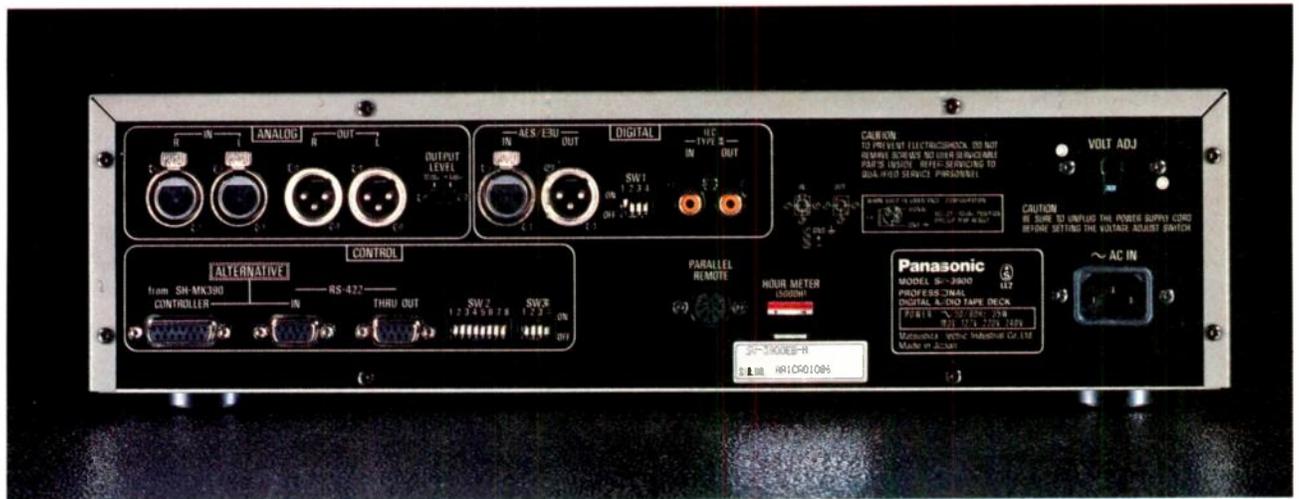
One of the lead ingots found in a Roman ship sunk near Sardinia showing the manufacturer's mark.

Collaboration will also extend to use of trace element and isotope analysis to identify the precise origin of the lead ingots. It would be intriguing indeed if the same lead which has lain useless for 2000 years could tell us about the history of the Roman Empire and also about the radioactive processes in the Sun which have played an even more fundamental role in our past.

Protected from environmental radiation by some 30m of water, the lead will provide valuable low-background shielding for precision physics experiments.

Photo: Cern Photo





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ES-BUS AND SERIAL CONTROL PROTOCOLS.

Such is the versatility of the SV-3900, it can be used equally successfully to record music or as a scientific research tool. You can, for example, interface it with a wide variety of digital devices - CD players, workstations, recorders. Or, alternatively, it can be networked with up to 31 other SV-3900 DAT machines. (To achieve this you can use either the RS-422 industry standard computer interface, or the optional SH-MK390 remote controller)

Communication on ES-bus and P2 interface is two-way. All tape and transport modes and functions can be controlled by computer, which in turn can receive and act upon technical and diagnostic information imparted by the SV-3900. Absolute/program times, counter number, error rates and the sampling frequency setting can all be read by the control computer.

With suitable software, the potential applications are almost limitless.

You could for example compile an overnight radio broadcast by using pre-recorded material from one machine, library selections from another and then patch into network news broadcasts at the appropriate times. (It goes without saying of course that traditional eight track cartridges are a thing of the past.)

Other less obvious applications include sophisticated telephone call management, data capture and satellite radio broadcasting. And because any sort of digital information presented in IEC II or AES/EBU format can be handled, the SV-3900 can even be used as a data recorder for remote applications such as monitoring oil flow in pipelines. (Information could be downloaded over the phone, or other network.)

Analogue data logging is of course possible using balanced inputs between -14dBu and +26dBu with >92dB dynamic range.

ONE-BIT ADCs.

Naturally the SV-3900 also offers stunning audio performance. One-bit ADCs linked to 64X oversampling anti-aliasing filters mean a complete absence of zero-cross distortion, and ensure total transparency and lucid detail at both high and low levels.

Similarly, the high resolution 4DAC system ensures low distortion and enhanced linearity at low levels on playback. Other useful touches include an error rate display (on-machine or output to the control computer) to keep you informed on the condition of tape and heads. A new tape transport system that allows access to any point on a two hour tape within 27 seconds. And, as you'd expect, sampling rates can be switched between 32, 44.1 and 48Khz.

The list of features packed into this machine is truly remarkable. But go down to your Panasonic dealer and you'll find the most impressive feature of all is tied on with a piece of string. A price tag of around £1300.



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CIRCLE NO. 128 ON REPLY CARD

Solid state outshines gas lasers

Solid-state lasers have many advantages over older gas-laser tubes such as robustness, low voltage operation and potential for a very long life. They are also at least two orders of magnitude more compact. But there have been technical problems with generating high powers and/or shorter wavelengths of light in the solid state devices.

However in the last few months several papers have been published indicating these limitations may soon be overcome, enabling solid-state lasers to occupy an increasing slice of the territory formerly occupied by the gas laser.

A group from the University of Illinois at Urbana-Champaign and EG&G Optoelectronics in Vaudreuil, Quebec, have reported (*Electronics Letters*, Vol 27, No 21) development of a solid-state room-temperature infra-red laser capable of producing a 5W CW output at a wavelength of 1064nm. Such high power output from a single 100µm stripe represents an order of magnitude improvement on previous quantum well laser diodes operating at 1064nm.

The laser structure consists principally of a 70Å InGaAs quantum well surrounded by 1000Å GaAs barriers and optically confined in AlGaAs cladding layers. The whole assembly, together with facet coating, is mounted on a metallised diamond heat-sink for CW operation.

Room-temperature light vs current characteristic shows a rise to 5.25W at 9A before catastrophic facet damage occurs. Under pulsed conditions (200ns and 1kHz) 25W output can be achieved at a current of 40A.

The team are confident that where high coherence and high wavelength stability are not critical factors, solid-state devices could well replace Nd:Yag lasers for many applications. Unlike the latter they would be cheap, small and easier to modulate.

8.5W visible from monolithic array

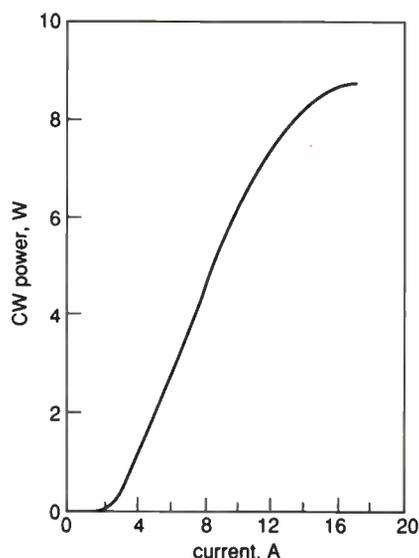
Producing shorter wavelength visible light is one further constraint on the designer of solid-state lasers. Without incorporation of quantum well active layers, designers would still be restricted to IR wavelengths and impossibly high lasing threshold currents.

In the same issue of *Electronics Letters*, a group from Spectra Diode Laboratories in San José, California, report development of a 680nm (red) laser diode that will generate 1W CW from a single 100µm-wide active layer based on a GaInP quantum well. As with the IR device above, it is bonded p-side down to its heat-sink. Minimum threshold current is 350A/cm² and efficiency is 38%.

The same team have taken this approach a stage further and fabricated sixteen 50µm emitters across an 8mm bar. This monolithic assembly, with emitters spaced every 500µm is capable of 8.5W output, limited principally by thermal considerations. The only other consequence of this multi-emitter approach is that the spectral band-width is broadened from the 2nm of a single emitter to around 4nm.

Into the blue

Applied Physics Letters, September 9, reports how Michael Haase and his colleagues at 3M in St Paul, Minneapolis have managed to create a solid-state laser capable of emitting light at 490nm. The blue-green emission is believed to be the shortest wavelength radiation ever generated by a solid-state laser.



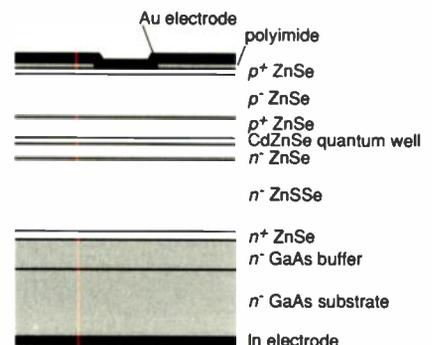
The blue-green laser diode is based on zinc selenide which has the necessary band gap to generate light in the blue-green part of the spectrum. There have, however, been enormous practical difficulties in the making of a functioning laser, not least the problem of fabricating the now-inevitable quantum well. The figure shows the structure of the prototype, capable of producing pulsed emissions at 490nm when held at liquid nitrogen temperatures. At room temperature the colour of the light becomes a little greener at 500nm.

But a convenient, efficient, blue solid-state laser is still many years away. The 3M device has a high lasing threshold and, being relatively inefficient, generates large amounts of potentially self-destructive heat. Nevertheless, observing all the work currently going on – as well as the insatiable demand for high capacity transmission links and data storage – it seems we will not have to wait long before solid-state lasers replace low to medium power gas devices for virtually all industrial applications.

Research Notes is written by John Wilson of

Fig. 1. Light output as a function of input current for 8mm monolithic array of 50µm emitters on 500µm centres.

Fig. 2. Cross section of the blue-green laser diode.



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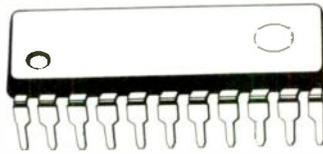
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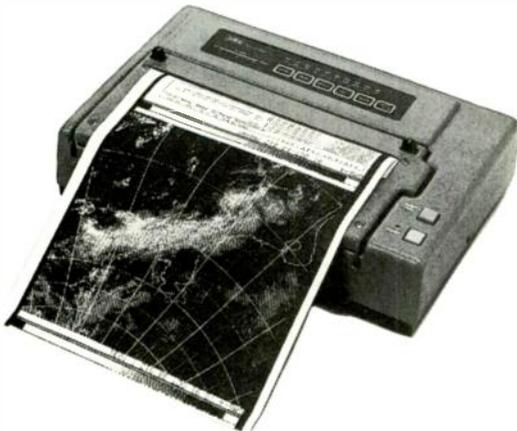


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Radio Facsimile Terminal WX-2000

The WX-2000 is a stand alone radio facsimile terminal designed to produce hard copy images from various facsimile services including Weather charts, Maps, News media and even Satellite pictures from NOAA, GOES and METEOR etc. The WX-2000 simply requires an audio signal from a shortwave or satellite receiver capable of receiving facsimile signals. The built-in high resolution (8 dots per mm) thermal line printer produces crisp images with high resolution. The WX-2000 is also capable of simulating grey scale which is ideal for Automatic Picture Transmission by weather satellites.

In addition to the basic functions, the WX-2000 provides full operational controls such as Auto Start, Sync. Adjustment, Position Alignment, Tuning LED etc to produce the highest quality images. The power requirement is 12 - 13.5V DC @ 3A, this makes the WX-2000 ideal for both on land and off shore applications.

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 Auto start: APSS type
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 Reception speed: 60, 90, 120 & 240 rpm, selectable
 Collaboration factor: 576 or 288
 Power requirements: 12 - 13.5V DC @ 3A
 Size: 310mm (W) x 70mm (H) x 200mm (D)

Full details available upon request

CIRCLE NO. 105 ON REPLY CARD

INSIDE INFORMATION

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CIRCLE NO. 106 ON REPLY CARD

The fluxgate magnetic sensing head is an extremely sensitive detector of magnetic fields. These cover from tiny field probes, no larger than 0.03 inches in diameter, through current probes, impurity detectors, compasses, metal locators, prospecting equipment, even to submarine detectors. Granted, not many people will wish to detect submarines but how many underwater diving enthusiasts would love to have a "diveable" hand-held wreck-finder?

The compass designs presented here, though carried out in detail and mostly tested, are primarily intended as illustrations of the technique and suggestions for experimentation. Considerable scope exists for variation and final presentation or even use of the basic signals made available.

An earlier article (*EW & WW* September 91) entitled *A Simple Magnetometer* described the principle and use of a fluxgate sensor to produce an earth field measuring device sensitive enough to detect the influence of solar flares on the ionosphere.

It determined the magnitude of two horizontal field components at right angles to one another. Given that information, it is obvious that one can calculate the direction of the principal horizontal component, which is precisely what we ask a compass to tell us.

The magnetometer, however, needed to detect very small variations in the field to fulfil its proper function and consequently needed a high signal to noise ratio. A compass makes no such demands, happily coping with a much lower signal to noise ratio and allowing the circuitry to be even simpler than before. Three common integrated circuits suffice for the sensor conditioning and in the simplest case, the output indicator need be no more than a centre-zero meter.

The simplest systems could well be regarded as the poor man's autopilot since if the pilot is considered to be the device closing the feedback loop, that is exactly what it is. If you are steering a boat or flying an aeroplane, all you really need are steady-as-you-go turn left/turn right instructions to maintain a heading.

The technique has much to recommend it as the equipment is minimal and hopefully therefore more reliable and the steer-



The technology described here lends itself to nautical and aeronautical navigation either as a direct reading compass or the sensing heart of an autopilot. The system could equally well be adapted to providing directional information for deaf people.

By Richard Noble.



ELECTRONIC fluxgate compass

ing arrangements if properly arranged are non-confusing, key elements in safe navigation.

Sensor circuits

The presence of an external magnetic field passing through a toroidal core produces an asymmetry in the magnetic induction waveform in the core. The previous design exploited the subtly changing widths of the less noisy pulses produced by induction in a sense winding over the two legs of the core.

This design is less fussy and simply extracts the even harmonics produced by the asymmetry and, in particular, the second harmonic of the switching frequency. A rather crude resonance with the sense winding also enhances the size of the signal being sought.

The core, as before, is a tape wound toroid of HCR alloy, designed by Telcon Metals for magnetic control systems. This is wound with approximately 170 turns of 0.5mm enamelled wire to provide a switching primary winding. The drive circuit, shown in

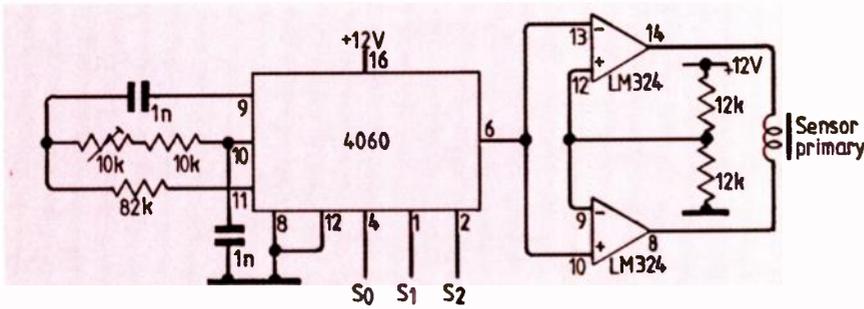


Fig. 1. The driver circuit used in all version

Fig.1, is provided by two of the operational amplifiers in an LM324 quad package working in a push-pull configuration. The input is a square-wave at the fundamental frequency of approximately 110Hz. This is provided by a 4060 cmos oscillator and divider chain which also supplies the second harmonic switching pulse for the phase detector from an appropriate tapping. This is needed because, although the second harmonic sensor signal varies as the external field, there is an abrupt change of 180° in the phase as the field reverses through zero, calling for a synchronous phase detector to preserve polarity correctly.

Returning to the drive system, the square-wave input does not produce a square-wave output voltage across the primary. Before the flux in the core reaches saturation, the primary core has inductance but at saturation the inductance collapses to zero and at this point the output voltage also disappears,

producing an output waveform like that shown in Fig 2a. This does tend to warm the integrated circuit chip, but is within the short circuit protection capability of the device and makes the circuit delightfully simple. The frequency of the oscillator is adjusted to make the output waveform as symmetric as possible so as to avoid the transformer coupling even harmonics into the pickup winding. Figure 3 shows the detector circuit.

The pickup winding is a single 500 turn winding of 0.2mm wire over the outside of the core, roughly resonated with the 10µF paper capacitor and fed to a unity gain amplifier which can have its phase reversed by 180°. The phase reversal is controlled by the analogue switch which either shorts the non-inverting input to ground or does nothing depending on its control voltage. When it is shorting to ground the circuit becomes a unity gain inverting amplifier. When it is open, the amplifier has a gain of -1 from the

inverting input and +2 from the non-inverting input. The net result is a gain of +1.

When the control is switched at the second harmonic frequency and in the appropriate phase, the amplifier neatly rectifies the signal and correctly converts the 180° phase change into a polarity change. In this way the DC output is a proper 4-quadrant vector component with a one-to-one correspondence to the equivalent earth field component. Two windings at right angles to each other will allow the reconstruction of an electric vector simulating the horizontal magnetic vector.

Idealised waveforms illustrating this process are shown in Fig. 2. All that remains is to amplify and smooth the rectified half sinusoids in an integrating circuit, the time constants chosen allowing some control over the damping of the instrument output. An oscilloscope will not show waveforms like the illustration because the signal is small and swamped by the interfering unbalanced signals. However if the external magnetic field is increased considerably then something much more like the idealised version can be seen. This is easy to do with a small bar magnet, held close to the sensor core, giving an increase in field strength of several orders of magnitude.

Fortunately the interfering signals which spoil an oscilloscope image have no effect on the final output and a large voltage swing is obtained for the tiny 0.18 gauss horizontal component of the earth's field.

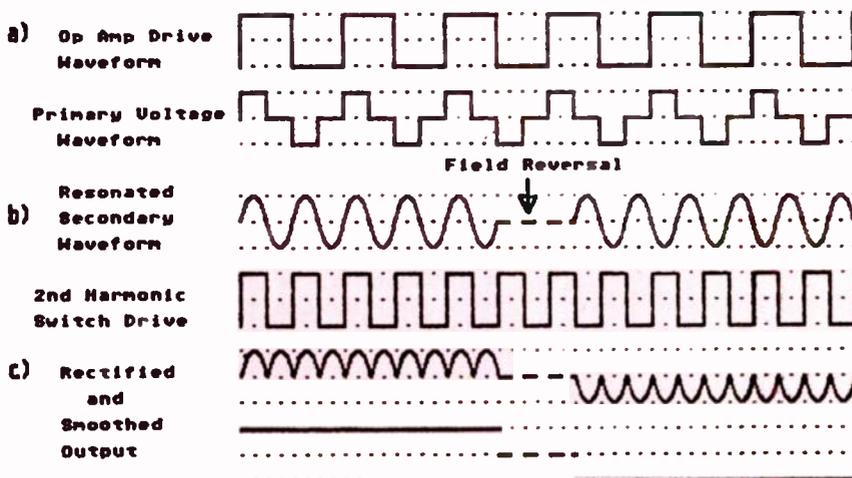
The output from this single channel device is fed to a centre-zero meter. When the axis of the sense winding is at right angles to the earth's field the meter reading is zero. Any departure from this orientation will make the meter deflection positive or negative, providing a heading error indication. The sense of the correction can be chosen to provide a steer left/steer right type of display. By rotating the sensor to the desired angle relative to the vehicle, the instructions to steer, if followed, will eventually bring the vehicle on to the correct heading as the meter reading approaches zero. Maintaining the zero reading will maintain the vehicle heading.

Heading-set mechanism

The following is a suggested design requiring no special tools and may obviously be improved upon by those with special facilities.

Fig. 4 (on p18) shows an exploded diagram of the parts and their method of assembly as made by the author.

Fig. 2. Idealised fluxgate waveforms



Setting and calibration

The more observant reader may be wondering about what looks like an anomaly at the octant boundaries. The analogue x or y value barely changes as the octant code switches suggesting that the two different outputs correspond incorrectly to the same angle. However this is no different to what happens at any other threshold. In reality there are a number of lamps all spaced equally around a circle and only one is ever showing at any time; it is only necessary to point that one in the right direction. In fact the sensor can be placed in any orientation as long as the dial is fixed to the indicator in the right place.

This is most noticeable in the simple 8-point compass. No one really wants a compass that indicates NNE, ENE, ESE, SSE, etc. The sequence N, NE, E, SE, S, etc is much more acceptable and in boxing the compass the adjustor will naturally make this happen. What he actually does is offset the zero octant boundary by around 22° so as to make north appear in the middle of the lamp's "on" range. In the same way the 72-point compass will be off by 2.5° and the 360-point version by 0.5°, though the latter is almost certainly masked by the precision limits of the system.

A reasonable target to aim for would be ±1° though this may not be achievable without considerable care. Certainly the second pickup winding on the sensor will have to be wound over a separate card or plastic sleeve to allow for some small adjustment during calibration. After the best position has been found it can be glued or varnished into place. The best position is that for which the zero-crossing points of the x and y signals are genuinely at right angles to one another.

Prior to checking this the amplifier zero offsets must have been set to ensure that the maximum excursions of the x and y signals are symmetrically disposed about zero volts. Some iteration of these adjustments may be necessary as they are interactive.

All of the above should be carried out while keeping the core in the horizontal plane though this need not be more complicated than temporarily securing it to a circle of card with blue-tack. If the card is first marked with a set of 15° protractor type markings and rotated over a cross marked on a flat surface the results can be reasonably accurate.

Subsequently the channel gains should be adjusted to match exactly the input span of the bar driver or A/D converter, whereupon the compass display should read correctly. Final tweaking may be beneficial while rotating the card over the cross to check the readings at 15° intervals. Once installed, careful checking in the usual manner is essential as navigation is sometimes a life-and-death matter and at this stage no effort is too great to ensure accuracy and reliability. Unless a good location can be found for the sensor the use of a deviation chart is recommended.

The final fitting is left to the ingenuity of the installer, but should be such that the sensor is horizontal in the normal cruising attitude of the vehicle and reasonably removed

from the influence of ferrous metal. In the case of a sailing boat, the first requirement means at least a fore and aft gimbal pivot to counter the vessel's heel. With an aeroplane, gimbaling is pointless as apparent gravity can be markedly non-vertical in manoeuvres and a fixed mounting is all that is required. The usual "northerly turning error" will be present but, unlike a normal compass, no violent swinging results and the indicated reading becomes smoothly stable as levelling occurs.

Direct reading remote compass

At the cost of some additional circuitry, the sensor can be mounted remotely in an iron-free area and the display fitted in any convenient position. The sensor electronics need an extra LM324 operational

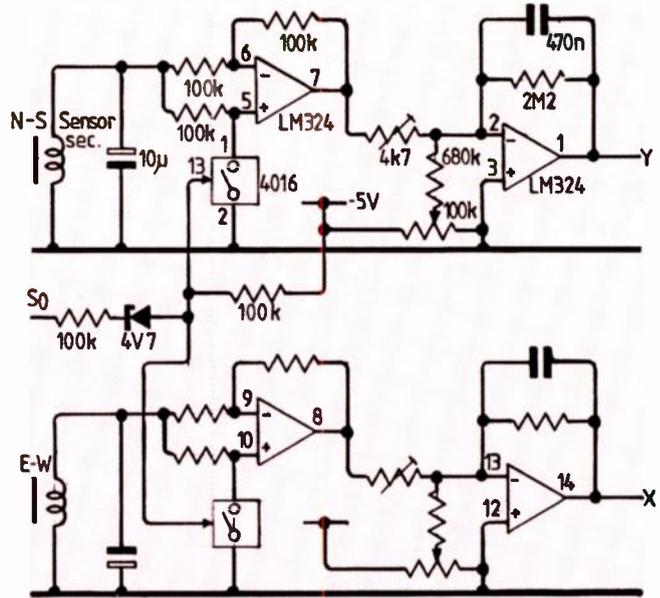


Fig. 5. Twin sensor circuit

amplifier chip to provide a second channel as shown in Fig. 5.

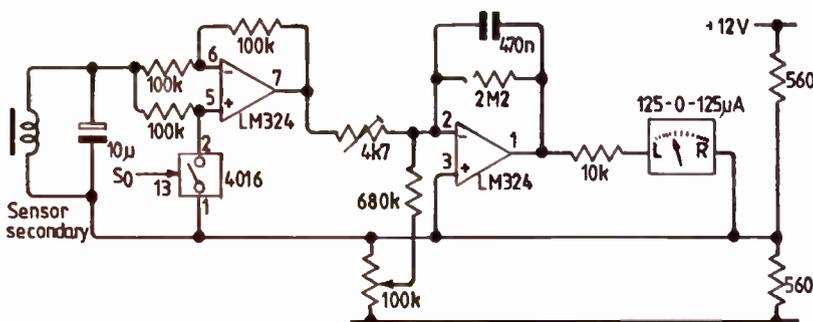
The sensor is wound, like the magnetometer version, with a second 500 turn pickup winding at right angles to the first. The electronics then provides two output signals, for convenience referred to as x and y, which represent the vector components of the horizontal magnetic field. From this point many different options are available to convert the signals into a display, with the usual tradeoff between precision, cost and complexity.

Before going into detail, however, it is instructive to examine the basic properties of the signal information the sensor system provides. The first obvious and familiar one is that the angle the magnetic vector makes to the axes is the arctangent of the ratio of x to y. One approach therefore would be to convert the analogue signals to digital and feed them to a single board computer. An eeprom stored program written in assembler or a higher level language such as compiled Basic or Forth could solve for the arctangent and send the output to a port fitted with a three digit liquid crystal display. Using a chip such as the Motorola 68705R3 it could even be a single chip computer. To those with the ability to put together such a combination and program it, this is probably the most straightforward solution and can have additional options incorporated such as stored way-point lists for a flight plan or sailing pattern.

For a more subtle solution, a close look at the basic properties suggests some intriguing alternatives. At the very lowest levels, the signals range through both polarities and a glance at Fig. 6a reveals that the polarity combinations are a code for the quadrant the vector resides in, ++ for 0 to 90°, +- for 90 to 180° and so on.

Another simple property is that the abso-

Fig. 3. Detector circuit for "steer-on-heading"



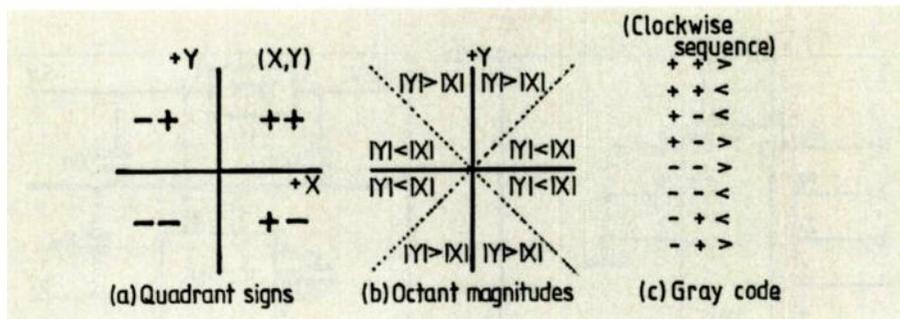


Fig. 6. Mapping out the octants with translation to Gray code equivalent

lute magnitude of x is either greater than that of y or vice versa, most of the time. Fig 6b reveals that this binary feature provides a third coded contribution increasing the resolution from quadrants to octants, $x < y$ implying 0 to 45° for example in the first quadrant. All of which makes good sense as three bits exactly codes eight states.

Additionally it should also be noted that in one of those delightful accidents of nature the code developed this way falls into the class known as Gray codes, namely sequences in which the state transitions are marked by single bit changes. Our encoded output never gives false or ambiguous readings as the values change, simply because there is only ever a single bit changing at any time. All this, without any deliberate design effort!

The underlying idea is also very easy to implement electronically. Two more LM324 amplifiers will provide comparators delivering the first two sign dependent bits. The absolute magnitude circuits are just two more again, with a handful of identical resistors and some diodes. The outputs go to yet another comparator which outputs the third bit and the job is done. The greatest cost is probably the circuit board which the parts are soldered to.

Simple 8-point compass

At this point the first somewhat crude compass display is possible as in Fig. 7. The three coded bits are used as the address inputs to a 4051, 3-to-8 line analogue switch and the outputs are connected to eight leds arranged in a circle (in the straight numeric order to decode the Gray code, of course). The result gives a heading indication of eight directions with a precision of $\pm 22.5^\circ$. This may not seem very good, but is entirely adequate for a road vehicle, to give one that comforting feeling of definitely heading in the right sort of direction when more or less lost. It should also be remembered that so far the analogue properties of the x and y signals have not even been considered. This gives a strong feeling that taking even a little notice of the analogue features should permit a major step forward.

One last convenient accident remains to be exploited. Between 0 and 45° the sine function is almost linear. A best fit line can be found for the ten points at 5° spacing by linear regression and this linear function used instead of the sine. The worst angular error

is 1.3° at the 45° position and all the others are less than 1°, averaging about 0.6°.

Over this angular range the analogue x signal is theoretically a sine function of the angle being sought after, so a linear interpretation of its analogue value will give a low-error solution. Over the range 45 to 90°, the y signal is theoretically a cosine function of the angle, which is just the sine of 90° minus the angle and therefore has the same convenient linear properties. The electronic implementation is obviously to transform the x and y signals into the first quadrant and use an analogue-to-digital converter to create the increased resolution. The first part needs no components, because it already exists in the shape of the absolute magnitude circuits introduced earlier. Two alternatives exist for the second part, one for the analogue enthusiast, the other for those who like digital displays.

Analogue 72-point compass

The analogue version, Fig. 8, uses an LM3914 led bargraph driver in dot mode to drive nine led cathode lines, the anode lines being multiplexed as eight common anode lines, one for each octant. These octant switches are provided by a 4051 1-pole 8-way analogue switch decoding the 3-bit octant code derived earlier. The input to this A/D converter system needs to be switched between the x and y signals at the octant

boundaries, but again no components are required because there is still one amplifier and two analogue switches left over in previously used chips and the driving signal is just the third bit of the already available octant code. This economically consumes all of the remaining spare parts.

The leds are arranged in a circle at 5° intervals and result in a display with $\pm 2.5^\circ$ precision and a worst error of about half that. Admittedly 72 leds are required, but bulk buying reduces the cost to no more than that of the digital version and some traditionalists just hate digital displays anyway.

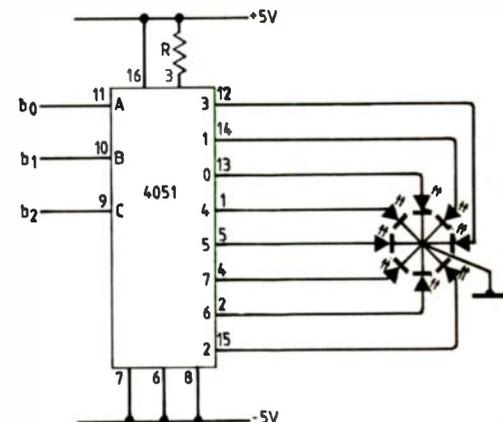
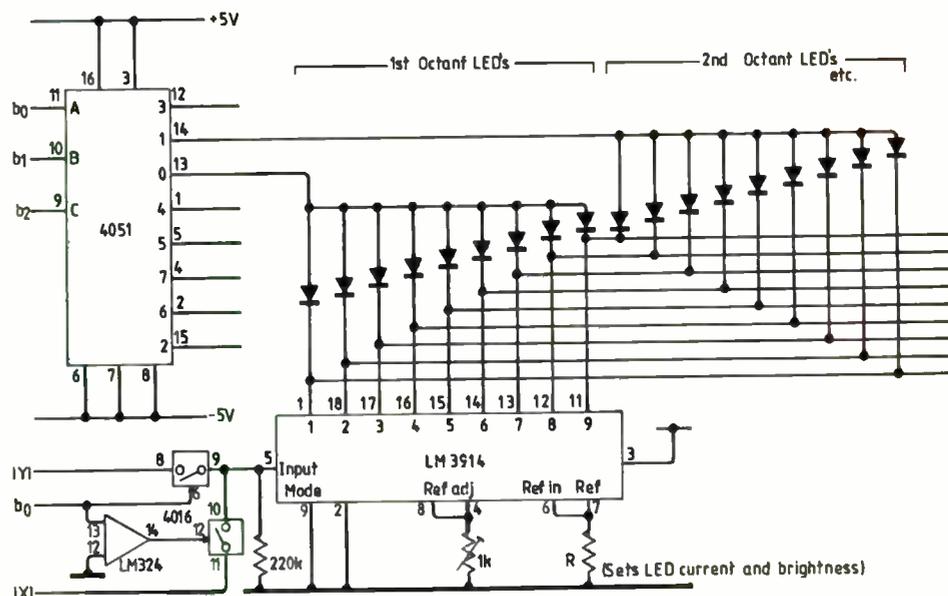


Fig. 7. A simple octant compass display

Digital 360-point compass

To make a digital version, the bar code driver is replaced with a CA3306 6-bit A/D flash converter, all earlier circuitry remaining the same. This divides the 45° octant into 64 levels providing the opportunity to correct for the slight non-linearity of the sine function, while providing even higher resolution. The technique is to use the six output bits as address bits for an eprom, together with the three octant bits, which are used to segment the EPROM into eight regions. In this way



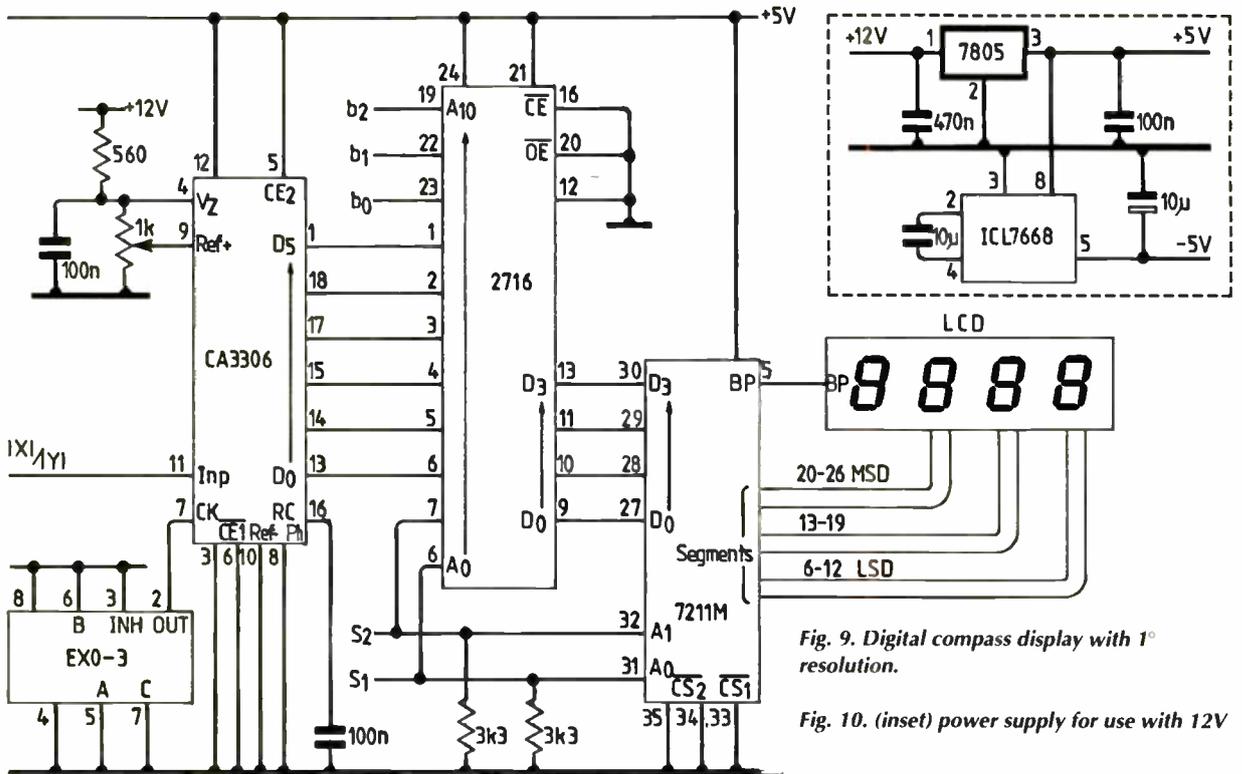


Fig. 9. Digital compass display with 1° resolution.

Fig. 10. (inset) power supply for use with 12V

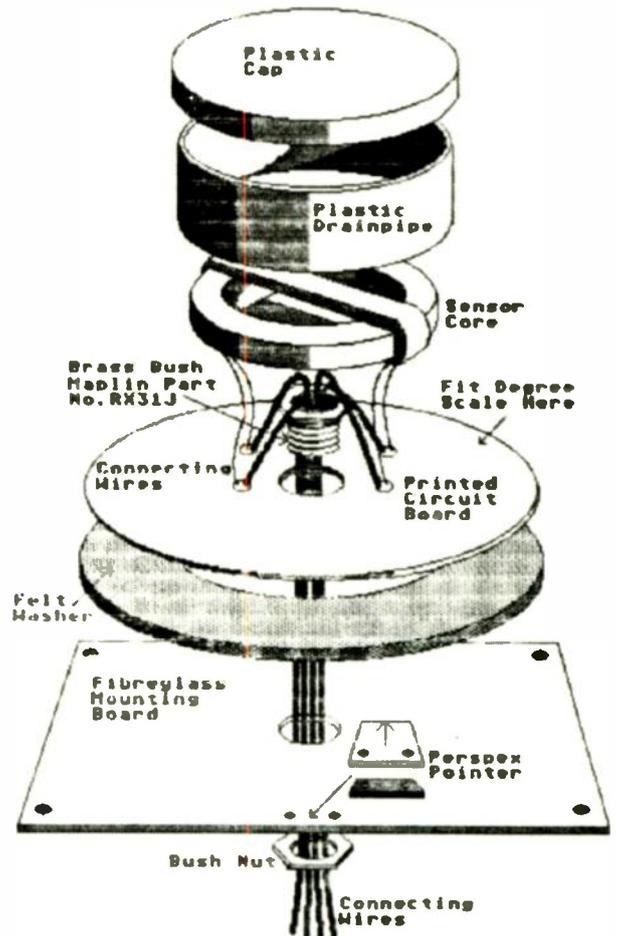
each combination of nine bits corresponds to a unique angle with a unique address, which can be programmed to output that angle to a display. Unfortunately the three digits needed for a compass display require twelve bits to code in BCD form and most eeproms are only eight bits wide.

The solution is to give each digit an address of its own and multiplex them continuously to an appropriate display by providing two more address bits from a slowly cycling two bit counter. The same two bits are fed to the multiplexing address lines of the display driver to synchronise the eeprom output to the digit position. A suitable display driver is the four-digit 7211M and the two bit counter needs no components as it already exists as the bottom end of the 4060 divider used in the sensor electronics. Bits 12 and 13 of this divider switch at approximately 7 and 3.5Hz respectively, giving a display update rate of about once per second.

Regrettably the serendipity of finding free parts just when they are needed does not extend to the 2MHz clock needed by the A/D converter. An EXO-3 crystal divider chip can be programmed to provide this. The 64 eeprom locations in each octant are programmed to deliver the nearest integer degree value to the exact value predicted by the sine function. The nineteen duplicated values scattered through the 45° range automatically provide the linearisation to give a 1° resolution.

There is no reason why the digital display cannot be inserted into the centre of the analogue compass rose.

Fig. 4. Head/sensor assembly as made by the author.



The Telcon 7a cores mentioned in this article are available directly from the author price £10.50. PCBs for driver and sensor circuitry are also available price £12 for the pair. Contact R & W Noble, Penbidwal House, Pandy, Abergavenny, Gwent NP7 8EA. Phone 0878-890367.

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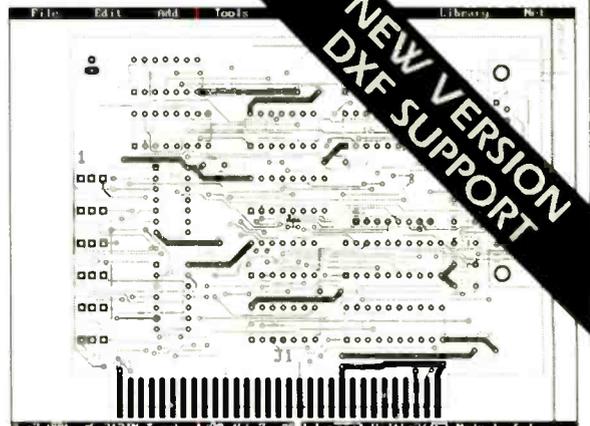
BoardRouter is priced at £295.00, which includes 3 months FREE software updates and full telephone technical support. BoardMaker and BoardRouter can be bought together for only £495.00. (ex. carriage & VAT)



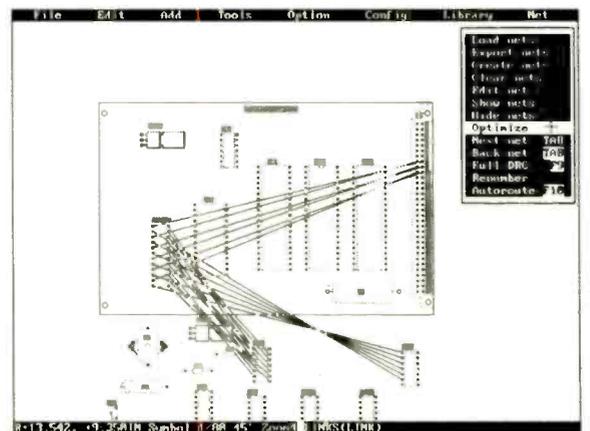
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BUYERS MARKET

shapes electronics cad sector

Supplier companies pulling out of cad and suicidal price cutting point to a sector in crisis? Yet the choice of packages is still wide. Steve Rogerson explores.

In the teeth of a recession there can be few areas in electronics and computing that are feeling the pinch worse than computer aided design. What was once the glamour sector of the market is today marked skirmishes that are ripping the industry to shreds.

But the range of packages available is still very wide, even in this "sector within a sector" of cad for electronics (though including universal design packages such as Autocad).

The design process splits naturally into two main functional areas; the first consists of electronics designers looking to arrange the various components to perform the required functions for a particular circuit. Next the components must be arranged on a PCB in a logical and cost-effective way, usually aiming to take up as little space as possible.

Electronic simulation is a middle stage between these two, taking the original design and running it like a real package to see if it works. Simulation is something of a side issue, especially for low-end PCB design where it is often too expensive. But for large system design it is essential. Typical packages include Susie and PSpice.

At the bottom of the market, costing between £100 and £200, are the straightforward drawing packages with restricted intelligence. They do serve a function, but there is usually no upgrade path and they can only be treated as a short term solution.

To buy something of real use, with intelligence in the package, tends to cost £1000 to £3000. Products in this band take information in the circuit diagram and use it to help design the PCB.

Users can make certain that all the tracks are associated with the right connections.

At the moment most designers of PCBs will be satisfied with this level of package, typified by products such as Pads-PCB. There are, however, many packages available – all with their own quirks and benefits and users should shop around to find which are the best fits for their applications.

Upwards from here are the fully featured packages that can cost up to £10,000 or even more. In general, the more you pay the more facilities you get.

Peter Chidzey from Cad Services explains the developing cad market: "Traditionally you had the drawing office with professional PCB design engineers. These are being replaced with electronics engineers who design the circuit and use the expensive packages to design the PCB."

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Susie PC-based logic simulation program simplifies digital design.

Integration of the various stages in the process is also very much the trend.

"People are going for more integration of packages from silicon design right the way through", says Chris Stevens from Computer Solutions. "They want the best simulator right through to the best autorouter. But the wise person buys it all from the same manufacturer rather than trying to do it themselves."

Price war

The cad industry, as mentioned earlier, is in something of a crisis. It has been hit hard by the recession and individual dealers have launched a price war that is lowering profit margins and driving some firms to the wall.

Others, like Lloyd Doyle, have pulled out of the market to concentrate on other areas.

In March this year Lloyd Doyle described itself in the *Cadcam 1991* catalogue as "the

UK's major distributor of the Pads suite of cad packages for PCB design."

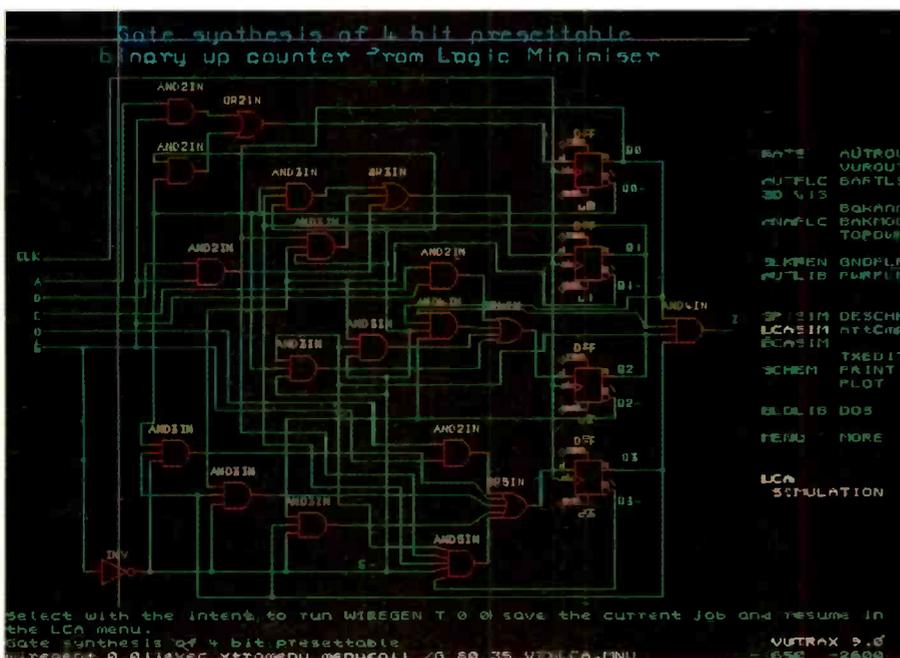
Six months later and that segment of business has been confined to the "what we used to do" file.

There is a fear in parts of the industry that the cad business is not professionally handled, perhaps even being a little "cowboyish". Some believe that the way the business is organised from above encourages competitiveness among distributors, while there is not sufficient control over territories and price. A result is the worry that there is "too much" cut pricing going on.

Chidzey agrees: "At the moment the market is pretty flat. There are a lot of people chasing a small amount of business and most people are suffering. There are very few companies in the last year who have made money out of PC cad. It has become very cut throat."

Vutrax equivalent logic of boolean equation for 4 bit presetable binary up-counter.

Picture: Those Engineers



PRODUCT SUMMARY

ALS-View II

ALS-View II is a menu driven tool for eliminating PCB replots. It lets designers read in any Gerber file for viewing, editing and printing check plots on various printers including standard 300dot/in laser printers. It runs on 386 or compatible PCs. Suppliers: ALS Design; ARS Microsystems.

Analyser III

Analyser III is a linear circuit analysis program that is suitable for analysing filters, amplifiers, crossover networks, wideband amplifiers, aerial matching networks, radio and TV IF amplifiers, chroma filters, and linear ICs. It runs on 386 and 486 PCs. Suppliers: Number One Systems.

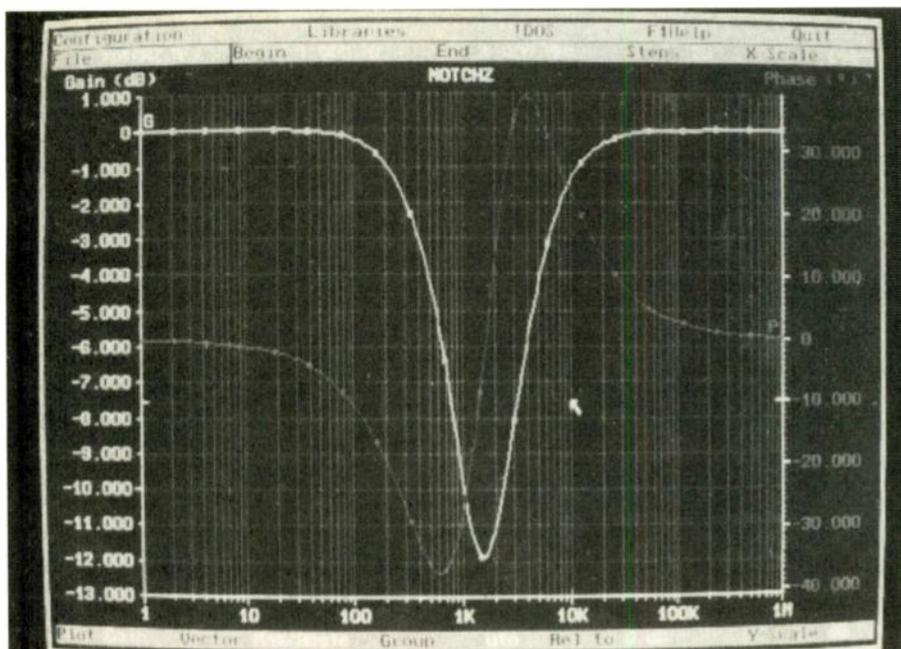
Ares

The Ares range of PCB design software comprises PCB II, Ares and Ares Autoroute all of which use a layout editor and the same graphical user interface as Isis. Suppliers: Labcenter Electronics.

AutoCad

AutoCad is a 2D and 3D professional computer-aided drafting and design package. It is the most widely used cad system in the world with more than 400,000 installations. In the electronics field it can be used for designing enclosures and can run on PCs and workstations.

Suppliers: Data Technology; Hawke Systems; KGB Micros; Option Circuits; SSI Microcad.



Analyser III linear circuit analyser runs on 386 and 486 machines.

Autotrax

Working from a net list, Autotrax automatically places components and routes tracks in conformance with user-definable design rules. Board layout can also be manually edited. Blocks of components can be defined, moved, rotated, flipped or copied while connectivity is maintained.

Suppliers: JAV Electronics; Protel Technology.

Bitspice

Bitspice is a smaller version of the LCA1 logic simulator program. Schematic input is available as an optional extra.

Suppliers: Those Engineers.

BoardMaker

BoardMaker is a PCB cad system with mouse driven pop-up menus and windows to make it easier to use. Features include schematic capture, graphical and manual netlist entry, design on the fly, components placement, routing, design rule checking, top down modifications, and symbol libraries.

Suppliers: Tsien.

Cadstar

Cadstar is a suite of programs that includes schematic capture, PCB layout and routing, and advanced routing. The library has more than 5000 digital and discrete parts including ansi and IEEE standard schematic symbols. It works on PC based platforms.

Suppliers: Option Circuits; Racal-Redac.

Cam-Bridge

Cam-Bridge is PC-based cam software for linking PCB design and fabrication. It allows prototyping without replots, uncovers design and house-keeping errors, and ensures correct preparation of artwork.

Suppliers: ARS Microsystems; ALS Design.

Codas

Codas runs on a PC and is a tool for designing control systems. It is aimed at single-input and single-output systems; for example position controllers such as those used on large telescopes. Basically, it controls the use of servo motors.

Suppliers: Golten & Verwer.

Colorcam

Colorcam is a flexible PCB design package with a systems resolution of 0.001mm. It can accommodate any component - from SMD to conventional - with any pitch. There is no restriction on the number of components, pad shapes or track widths. It is supplied with a library and comes either as a manual design package or in modules including schematic capture and autorouting using the T414 transputer.

Suppliers: LPKF; Tracks.

Dazix SDE

Dazix SDE is a synthesis design environment for the capture and synthesis of asics including PLDs, FPGAs, and ECLs. Designs can be described using any combination of entry methods including Boolean equations, truth tables, state machines, bubble diagrams, VHDL and schematics.

Suppliers: Dazix Intergraph.

Design Framework II

Design Framework II is a composition of a number of tools that provide complete design flows for IC, PCB and asic designers. Front end tools for design capture and simulation are the same for each technology, but physical layout programs are specific to the target technology.

Suppliers: Cadence Design Systems.

Easy PC

Easy PC, winner of a 1989 British Design award, is PCB design and schematic drafting cad software of which more than 7500 packages are in use around the world. Circuit diagrams and PCBs can be produced from the same package. It is aimed at 286 and 386 machines, but will also run on slower 8086 PCs.

Suppliers: Number One Systems.

Easytrax

Easytrax is a PCB design system that can run on PCs or Macs and includes pen plot, Gerber photoplot, N/C drill and PostScript capabilities. It is an entry level package.

Suppliers: JAV Electronics; Protel Technology.

ECA2

ECA2 is for analogue circuit analysis. It has a lot

of power, but people who want the flexibility on smaller circuits may be better off with its little sister Spiceage. Both will handle digital circuits but not as quickly as LCA1 and Bitspice from the same family. Schematic input is available as an optional extra.

Suppliers: Those Engineers.

Ecad Plus

Ecad Plus is software for simplifying and speeding up the development of electrical, electrotechnical and electromechanical drawings and projects. Using the package, a user can develop on a PC a multi-sheet project including drawing phase and related literature.

Suppliers: ARS Microsystems; Microdata System.

EEDesigner

EEDesigner is an electronics design package that does schematics, simulation and PCB layout. It runs on the PC and is a fully integrated package for electronics, cad and cae. Powerful integration between the component parts is a feature of the package which works with the Maxroute autorouter package.

Suppliers: Betronex.

Elcad

Also known as RDS40, Elcad is a database oriented cad/cae system for the documentation of circuit and control diagrams. The database is automatically loaded with data from the electric, electronics, hydraulics and pneumatic fields. Current path diagrams are drawn up graphically in interactive dialogue. It runs on 286 and 386 machines.

Suppliers: Rotring; SSI Microcad.

EPlan

EPlan is an electrical design package for the automotive industry and can be used for, say, running robots on a production line. It will run on Compaq computers.

Suppliers: Auto Metrix.

Flotherm

Flotherm is a thermal analysis cad package that uses computational fluid dynamics to predict the 3D air flow and heat transfer in an electronics system. It can simulate a complete set up from component to system level to help the designer work out the best ventilation methods.

Suppliers: Flomerics.

Fourier Perspective III

Fourier Perspective III is a complete digital signal processing environment with true menu selection. Applications include noise and vibration analysis, digital filter design, and financial analysis.

Suppliers: Laplace Instruments.

FutureNet-5

FutureNet-5 is a schematic designer for PC and Sun workstations. It includes a scripting language, layered database and help system. Other features include design rule checker, PCB translators, and back annotators.

Suppliers: Data I/O; Instrumatic; Option Circuits.

**CONTINUED
ON
PAGE 43**

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HP DC Current source type 6177C - £200.
HP Frequency comb generator type 8406A - £400.
HP Sampling Voltmeter (Broadband) type 3406A - £200.
HP Vector Voltmeter type 8405A - £400 to £600.
HP Synthesiser/signal generator type 8672A - 2 to 18GHz - £6000.
HP 8640A signal generator - OPT 001 - 002 - 5Mc/s - 1024Mc/s - £1000.
HP Oscillographic recorder type 7404A - 4 track - £350.
HP Plotter type 9872B - 4 pen - £300.
HP Sweep Oscillators type 8690 A & B + plug-ins from 10Mc/s to 18GHz also 18-40GHz. P.O.R.
HP Signal Generators type 612 - 614 - 618 - 620 - 628 - frequency from 450Mc/s to 21GHz.
HP Network Analyser type 8407A + 8412A + 8601A - 100Kc/s - 110Mc/s - £1000.
HP 432A-435A or B Power Meters + Powerheads - 10Mc/s-40GHz - £200-£650.
HP Down Converter type 11710B - 0.1-11Mc/s - £450.
HP Pulse Modulator type 11720A - 2-18GHz - £1000.
HP Modulator type 8403A - £100-£200.
HP Pin Modulators for above-many different frequencies - £150.
HP Power Meter type 435A (no head) - £150.
HP Counter type 5342A - 18GHz - LED readout - £1500.
HP Signal Generator type 8640B - Opt001 + 003 - 5-512Mc/s AM/FM - £1200.
HP Spectrum Display type 3720A £200 - HP Correlator type 3721A £150.
HP 37555 + 3756A - 90Mc/s Switch - £500.
HP Amplifier type 8447A - 1-400Mc/s £400 - HP8447F - 1-1300Mc/s £800.
HP Frequency Counter type 5340A - 18GHz £1000 - rear output £800.
HP Programmable pulse generator type 8161A - £1500.
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HP Signal Generator type 8660C - 1-2600Mc/s AM/FM - £3000.
HP Signal Generator type 8656A - 0.1-990Mc/s AM/FM - £2250.
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Racal/Dana Interface type 9932 - £150.
Racal/Dana GPIB Interface type 9934A - £100.
Racal/Dana Timer/counter type 9500 (9515 OPT42) - 1250Mc/s - £450.
Racal/Dana 9301A-9303 RF Millivoltmeter - 1.5-2GHz - £350-£750.
Racal/Dana Counters 9915M - 9916 - 9917 - 9921 - £150 to £450. Fitted FX standards.
Racal/Dana Modulation Meter type 9009 - 8Mc/s - 1.5GHz - £250.
Racal - SG Brown Comprehensive Headset Tester (with artificial head) Z1A200/1 - £450.
EIN 310L RF Power Amp - 250kHz - 110Mc/s - 50Db - £250.
Marconi AF Power Meter type 893B - £300.
Marconi Bridge type TF2700 - £150.
Marconi/Saunders Signal Sources type - 6058B - 6070A - 6055B - 6059A - 400 to 18GHz. P.O.R.
Marconi TF2015 Signal Generators - 10MHz - 520Mc/s - AM/FM - £250.
Marconi TF1245 Circuit magnification meter + 1246 & 1247 Oscillators - £100-£300.
Marconi microwave 6600A sweep osc. mainframe with 6650 PI - 18-26.5GHz or 6651 PI - 26.5-40GHz - £1000 or PI only £600.
Marconi distortion meter type TF2331 - £150, TF2331A - £200.
Marconi 6700B sweep mainframe - £200.
Thurlby converter 19 - GP - IEEE - 488 - £150.
Philips logic multimeter type PM2544 - £100.
Microwave Systems MOS/3600 Microwave frequency stabilizer - 1 to 18GHz & 18 to 40GHz - £1000.
Bradley Oscilloscope calibrator type 156 - £150.
Bradley Oscilloscope calibrator type 192 - £500.
Tektronix Plug-ins 7A13 - 7A14 - 7A18 - 7A24 - 7A26 - 7A11 - 7M11 - 7S11 - 7D10 - 7S12 - S1 - S2 - S6 - S52 - PG506 - SC504 - SG502 - SG503 - SG504 - DC503 - DC508 - DD501 - WR501 - DM501A - FG501A - TG501 - G502 - DC505A - FG504 - P.O.R.
Alltech Stoddart receiver type 1727A - 01-32Mc/s - £5000.
Alltech Stoddart receiver type 37157 - 30-1000Mc/s - £5000.
Alltech Stoddart receiver type NM65T - 1 to 10GHz - £3000.
Gould J3B Test oscillator + manual - £200.
Image Intensifiers - ex MOD - Tripod fitting for long range night viewing - as new - £1500-£2000.
Don 10 Telephone Cable - 1/2 mile canvas containers or wooden drum - new - Mk2-3 or 4. P.O.R.
Infra-red Binoculars in fibre-glass carrying case - tested - £100ea. also Infra-red AFV sights - £100ea.
ACL Field Intensity meter receiver type SR - 209 - 6. Plugs-ins from 5Mc/s to 4GHz - P.O.R.
Syston Donner Counter Model 6057 - 18GHz - £800.
Clark Air Masts - Heavy Duty - Type Scam - 40ft or 70ft - £200-£600.
Tektronix 491 spectrum analyser - 1.5GHz-40GHz - as new - £1200 + manual.
Tektronix Mainframes - 7603 - 7623A - 7633 - 7704A - 7844 - 7904 - TM501 - TM503 - TM506.
Knott Polyskanner WM1001 + WM5001 + WM3002 + WM4001 - £1000.
Alltech 136 Precision test RX + 13505 head 2 - 4GHz - £350.
SE Lab Eight Four - FM 4 Channel recorder - £200.
Alltech 757 Spectrum Analyser - 001 22GHz - Digital Storage + Readout - £5000.
Dranetz 606 Power line disturbance analyser - £500.
Precision Aneroid barometers - 900-1050Mb - mechanical digit readout with electronic indicator - battery powered. Housed in polished wood carrying box - tested - £100-£200-£250. MK1, 2 or 3.
B & K Sound Level Meter type 2206 - small - lightweight - precision - 1/2" microphone - in foam protected filled brief type carrying case with windshield & battery + books + pistol grip handle - tested - £170. Carr. £8. - B & K 2206 Meter + Mike + Book - less carrying case etc. - £145. Carr. £8.
DISCOUNT ON QUANTITY
HP 141T Spectrum Analysers. All new colours supplied with instruction manuals.
HP 141T-8552A or B - 8556A - 20Hz to 300kHz £2000 A - £2200 B.
HP 141T-8552A or B - 8553B - 1kHz to 110Mc/s. £1800 A - £2000 B.
HP 141T-8552A or B - 8554B - 100kHz to 1250Mc/s. £2050 A - £2250 B.
HP 141T-8552A or B - 8555A - 10Mc/s to 18GHz. £3250 A - £3450 B.
HP 141T - old colour mainframe + 8552A; 8553B - 1kHz to 110Mc/s. Instruction manuals - £1500.
HP 3580A LF-spectrum analyser - 5kHz to 50kHz - LED readout - digital storage - £1600 with instruction manual or £1750 with internal rechargeable battery.
HP5352B - 40GHz counter - Liquid crystal readout with instruction manual - £5000.
Spectrascope 11 SD335 (S.A.) real-time LF analyser - 20Hz to 50kHz - LED readout with manual - £850.
Tektronix 7D20 plug-in 2-channel programmable digitizer - 70 Mc/s - for 7000 mainframes - £500 - manual - £50.
Datron 1065 Auto Cal digital multimeter with instruction manual - £750.
Racal MA 259 FX standard. Output 100Kc/s - 1Mc/s - 5Mc/s - internal NiCad battery - with manual. £150.
Tektronix 2235 100Mc/s oscilloscope + two probes + manual. £800.
Tektronix 2465 300Mc/s oscilloscope + two probes + manual. £1600.

Tektronix 485 350Mc/s oscilloscope + two probes + manual £500.
Tektronix TR503 tracking generator - 10Mc/s to 1800Mc/s + manual - £1500.
Aerial array on metal plate 9" x 9" containing 4 aeriels plus Narda detector - .100-11GHz. Using N type and SMA plugs & sockets - ex eqpt - £100.
EIP 451 microwave pulse counter 18GHz - £1500.
Marconi RF Power Amplifier TF2175 - 1.5Mc/s to 520Mc/s with book - £100.
HP 8614A Signal Generator 800Mc/s to 2.4GHz - old colour - £300. New colour - £600.
HP 8615A Signal Generator 1.8GHz to 4.5GHz - old colour - £200. New colour - £400.
HP 8620A or 8620C Sweep Generators - £400 or £900.
Marconi 6155A Signal Source - 1 to 2 GHz - LED readout - £600.
Schlumberger 2741 Programmable Microwave Counter - 10Hz to 7.1GHz - £750.
Schlumberger 2720 Programmable Universal Counter 0 to 1250Mc/s - £600.
HP 37203A HP-IB Extender - £150.
PPM 411F Current Reference - £150.
HP 5363B Time Interval Probes - £150.
Marconi B057B Signal Source - 4.50 to 8.50 GHz - £300.
HP 8900B Peak Power Calibrator - £100.
HP 59313A A/D Converter - £150.
HP 59306A Relay Actuator - £150.
HP 2225CR Thinkjet Printer - £150.
TEK 178 Linear IC Test Fixture - £150.
TEK 576 Calibration Fixture - 067-0597-99 - £250.
HP 4437A 600 Ohm Attenuator - £100.
Marconi Signal Source 6059A - 12-18 GHz - £400.
HP 8006A Word Generator - £150.
HP 1645A Data Error Analyser - £150.
Texscan Rotary Attenuators - BNC/SMA 0.1-10-60-100DBS - £50-£150.
HP 809C Slotted Line Carriages - various frequencies to 18GHz - £100 to £300.
HP 532-536-537 Frequency Meters - various frequencies - £150-£250.
HP 3200B VHF Oscillator - 10Mc/s-500Mc/s - £200.
VAL Radio Inverters - 200-watt 12V to 115/230V AC 50c/s. £100.
Barr & Stroud variable filter EF3 0.1Hz-100Kc/s + high pass + low pass - mains - battery - £150.
Krohn-Hite Model 3343 filter - low pass, high pass. 0.1Hz-100Kc/s - mains - battery.
Krohn-Hite 4100 oscillator.
Krohn-Hite 4141R oscillator - 1Hz-10,000kHz.
Krohn-Hite 6880 programmable distortion ANZ-IEEE-488.
Krohn-Hite 3750 filter, low pass, high pass - .02Hz-20kHz.
Parametron D150 variable active filter, low pass - high pass - 1.5Hz-10kHz. £100.
S.E. Lab SM215 Mk11 transfer standard voltmeter - 1000 volts.
Fluke 4210A programmable voltage source.
Alltech Stoddart P7 programmer - £200.
Fluke 8500A digital multimeter.
H.P. 3490A multimeter.
H.P. 6941B multiprogrammer extender £100.
Fluke Y2000 RTD selector + Fluke 1120A IEEE-488-translator + Fluke 2180 RTD digital thermometer + 9 probes. £350 all three items.
H.P. 6181 DC current source. £150.
H.P. 59501A - HP-IB isolated D/A power supply programmer.
H.P. 3438A digital multimeter.
H.P. 61775 DC current source.
H.P. 6207B DC power supply.
H.P. 741B AC/DC differential voltmeter standard (old colour) £100.
H.P. 6209B DC power unit.
Fluke 80 high voltage divider.
Fluke 887AB AC + DC differential voltmeter.
Fluke 431C high voltage DC supply.
H.P. 1104A trigger countdown unit.
Tektronix M2 gated delay calibration fixture. 067-0712-00.
Tektronix precision DC divider calibration fixture. 067-0503-00.
Tektronix overdrive recovery calibration fixture. 067-0608-00.
Schwarzbeck EMC H.F. Interference measuring RX's. FSME 1515 - 85Kc/s-30Mc/s + FSME 1514 - 85Kc/s - 30Mc/s + 15141 + 15142 - loop aeriels - £500. Vume 1520A VHF-UHF 25-1000Mc/s - £500.
Avo VC 163 valve tester + book £300.
Gould 60000 XYT recorder £250.
H.P. 5011T logic trouble shooting kit £150.
Marconi TF2163S attenuator - 1GHz. £200.
PPM 8000 programmable scanner.
H.P. 9133 disk drive + 7907A + 9121 twin disk.
Fluke 730A DC transfer standard.
B&K level recorder 2307 + 2010 heterodyne analyser - in rack - £1000.
B&K 2971 phase meter - £150.
B&K 2112 audio frequency spectrometer - £100.
B&K 4815 calibrator head.
B&K 4812 calibrator head.
B&K 4142 microphone calibrator - £100.
B&K 1022 band FX oscillator - £100.
B&K 1612 band pass filter set - £150.
B&K 2107 frequency analyser - £150.
B&K 1013 BFO - £100.
B&K 1014 BFO - £150.
B&K 4712 FX response tracer - £250.
B&K 2603 microphone amp - £150.
B&K 2604 microphone amp - £200.
B&K 2804 microphone power supply - £200.
B&K 2019 analyser - £350.
Farnell power unit H60/50 - £250.
H.P. FX doubler 938A, also 940A - £300.
Racal/Dana 9300 RMS voltmeter - £250.
A.B. noise figure meter 117B - £400.
Alltech 360D 11 + 3601 + 3602 FX synthesizer 1Mc/s-2000Mc/s. £500.
H.P. sweeper plug-ins - 86240A - 2-8.4GHz - 86260A - 12.4-18GHz - 86260AH03 - 10-15GHz - 86290B - 2-18.6GHz.
Teleguipment CT71 curve tracer - £200.
H.P. 461A amplifier - 1Kc-150Mc/s - old colour - £150.
H.P. 8750A storage normalizer.
Tektronix oscilloscopes type 2215A - 60Mc/s - c/w book & probe - £400.
Tektronix monitor type 604 - £100.

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Marconi TF2008 Signal Generators 10Kc/s to 510Mc/s - AM-FM - off the pile - tested - working - £300. Not working or part-working - £200. Kit box of attachments - £25. All supplied with manual, quick test only given, working or non-working - fair looking condition - 300 only available. As new ones still available as normal, fully tested with box of attachments - £400-£500.
Clark Scam Heavy Duty 40 Telescopic Pneumatic Masts - retracted 7'8" - head load 40lbs - with or without supporting legs & erection kit - in bag + handbook - £200-£500.
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CIRCLE NO. 127 ON REPLY CARD

MLSSA brings speaker design in from the cold

Dave Berriman reports on a PC card which may help acoustic engineers dispense with open air or anechoic chambers for those critical loudspeaker measurements.

SYSTEM REQUIREMENTS

PC/XT or AT with 8087, 80287 or 80387 co-processor
640K
Floppy disk (but hard disk recommended)
MS dos or PC dos 2.1 or higher
Expansion bus speed of 8MHz or less.

Traditionally, acoustics engineers – and in particular loudspeaker designers – have relied on anechoic rooms or the open air to eliminate sound reflections and achieve accurate sound pressure level measurements. But swept frequency response test equipment is expensive, and anechoic rooms are costly to hire and inaccurate at low frequencies (below about 150Hz, except for the very largest rooms).

However elimination of reflections can also be achieved using fast FFT, and DRA Laboratories' MLSSA (pronounced Melissa) plug-in audio FFT analyser card and associated software will enable that complex analysis to be handled by the PC.

Reflections on measurements

Multiple reflections from room surfaces mean attempts to achieve accurate swept-frequency responses in ordinary rooms are fraught with danger. Bringing the microphone very close to the loudspeaker makes the direct sound dominant and allows quite accurate low-frequency tests to be made. But positioning the microphone at the traditional one metre measuring distance produces a response that can be all over the place.

A frequency-modulated "warble tone" can prevent build up of some of the standing waves and can smooth-out the more obvious dips and peaks, but this is more of a cosmetic than a real cure. Bringing the microphone closer makes investigation of crossovers feasible. But in this kind of work, where phase relationships and relative driver-to-microphone time delays are critical, careful interpretation of results is required.

Elimination of reflections is the only real answer. Tone-burst gating systems, such as Bruel and Kjaer's, achieve this by gating a sine-wave signal on and off and cutting off the measurement before reflections are received. Fast fourier analysis techniques can achieve the same ends, either using noise or transient impulses, such as square, or raised sin or cosine waveforms.

The Fast FFT for audio design was pioneered by Kef in the 1970s, who did a lot of work on measuring loudspeakers with impulses. Computing the FFT of the impulse from the speaker, and comparing this with the FFT of the loudspeaker's input pulse, produces phase and frequency responses. By cutting off reflections, these can be eliminated.

Kef plotted a series of frequency responses against a third axis (time) to create a waterfall graph showing output decay over a range of frequencies.

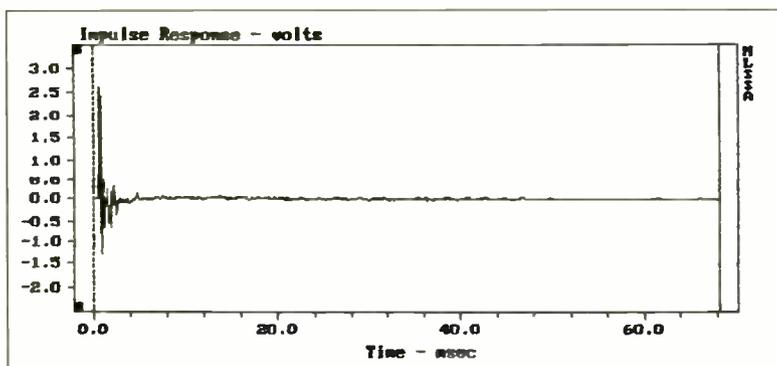
Computers then were expensive and bulky. Now packages such as Melissa bring that power to the PC.

Quite a card

Melissa is a maximum length sequence system analyser card for PCs.

The card will operate with quite small PCs, but if lengthy computations and file management are to be avoided a 286, 386 or 486 machine with co-processor and a hard disk, are really essential. The more powerful machines also give other advantages, especially if applications include comparing memory-hungry, high-resolution, low-frequency responses or lengthy time/energy

Whole impulse time response, as shown at acquisition.



curves. For these tasks, the improved memory-management available with 386s and 486s is invaluable.

A-to-D converter, programmable filters, signal generator and any additional hardware required are included on the Melissa board. All that is needed for a complete measuring system is a microphone, microphone amplifier and power amplifier. One disadvantage is that this makes for a cumbersome set-up, particularly when compared with the compact self-contained Neutrik 3300 sine-wave plotter – my design mainstay up until now.

But Melissa is a much more capable unit in many other ways. Unlike a conventional FFT analyser using random noise or generating a series of identical impulses, Melissa generates a kind of pseudo-random noise signal called the maximum length sequence. It sounds a little like throbbing, filtered white noise but is cyclic, not random.

Designers DRA Laboratories claims that as long as the analyser samples the complete sequence, there will be no truncation error. This contrasts with conventional FFT analysers which introduce a truncation error when the measurement is cut off. As a result, DRA says Melissa can achieve 1Hz resolution with a 10kHz bandwidth; or 1kHz bandwidth with 0.125Hz resolution if the whole sample is used.

Using fewer samples (by setting the acquisition length, chosen when the measurement is made) simply reduces frequency resolution. After data has been captured, it is converted from its noise-like origins, to display a conventional impulse response, similar to an ordinary FFT.

For a loudspeaker being measured in a room, the screen will clearly show loudspeaker output and decay plus any reflections. All reflections occurring after a certain time can be cut out by reducing frequency resolution to $1/t$, where t is the cut-off time. So the whole time-domain response can be subjected to FFT, giving the complete frequency and phase responses over the measured bandwidth, and resolution is limited only by the chosen acquisition length. Or an initial part of the time response can be selected, with a further reduction in resolution. Because the original MLS maximum length sequence is a "known" quantity, the analyser compares the MLS from the microphone to the original, and does not need to measure loudspeaker input. Thus, unlike a normal two-channel FFT analyser, Melissa requires only one measuring input.

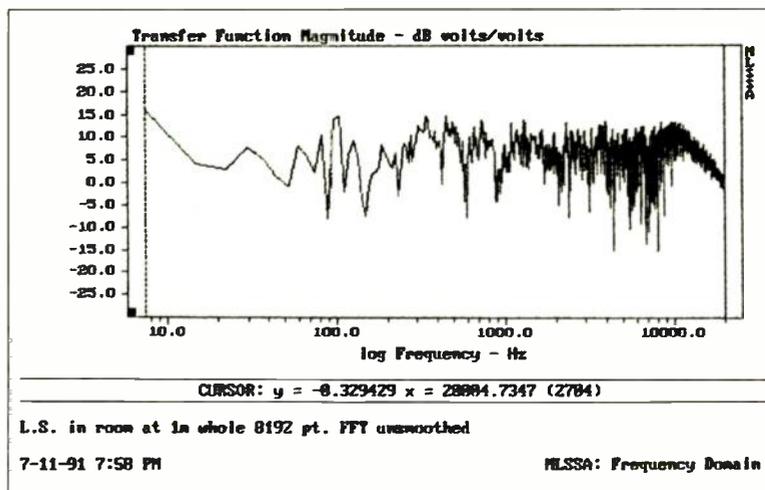
Acoustics speciality

Features have been designed with acoustics work firmly in mind. Of particular interest to acoustics engineers is the package's ability to cut short the analysed waveform, eliminating reflections from floors, ceiling and walls, creating a pseudo-anechoic response. The effect is achieved by moving the cursor and zooming in on the wanted section.

The result of executing the FFT on this time-slice is equal to a true anechoic measurement at high frequencies, but – as mentioned above – resolution will be reduced to $1/t$, where t is the time duration of the sample taken. For example, a cut off at 5ms to eliminate a ceiling reflection would result in a resolution of 200Hz, giving points on the curve at 200Hz, 400Hz, 600Hz... and so on.

Below 200Hz there is nothing. Melissa displays a curve between the points, and also plots a spurious line below 200Hz – which should be ignored. This is not so much a limitation as something which must be acknowledged when interpreting measurements.

A full catalogue of the package's abilities and their use in practice would need a very lengthy article (see box). But the great thing about Melissa is that just one measurement, or "acquisition" is required. Everything else is



post-processing and can be carried out later, at a different location and even on a different computer. So measurements could be made using a small monochrome machine, with processing carried out on a much more powerful colour computer for faster graph generation and a better display.

Melissa in practice

So much for the theory, what is Melissa like to set up and use?

Munro Associates, who distribute the package, normally recommend one of the Toshiba laptop computers (with 286 or 386 processor and co-processor) for portable systems, because they take the full-length card. Many laptops only take a half-length card, or none at all.

But for me, Munro located a Samsung S5200 – which also takes a full-length card and was available at a somewhat lower price. Munro also installed the board and was extremely helpful with subsequent queries.

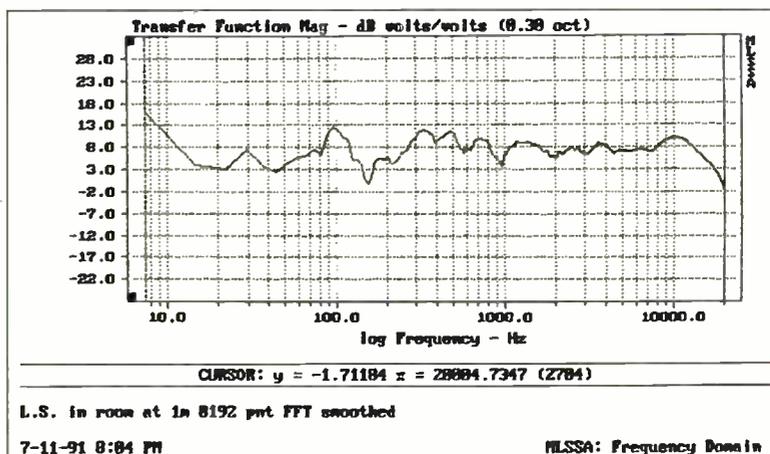
Once installed, Melissa works like a dream. Users must first find their way around the various menus and sort out the many functions. But that done the package really is easy to use, though you must read the manual before starting as the large choice of facilities and options available can cause confusion. However it is that range of facilities that gives Melissa such versatility.

For instance, after capturing the step-response "impulse", use cursors to decide which part is needed, zoom in then just press F followed by E (FFT EXECUTE). After a few seconds the FFT appears, viewed as it comes, or smoothed to whatever fraction of an octave is desired.

Press W and Melissa constructs a waterfall. On the

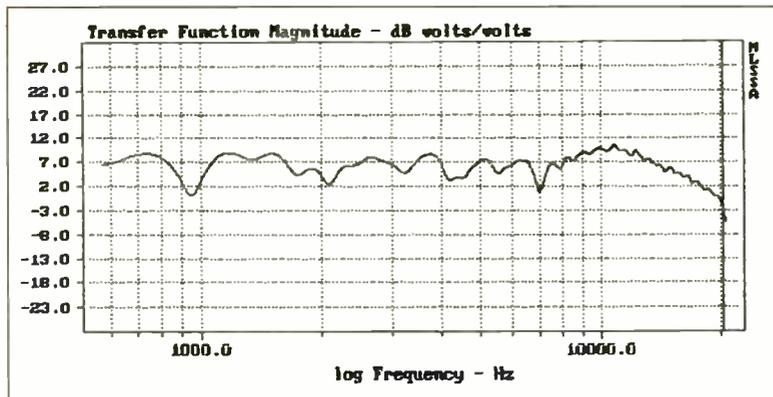
The whole 8192 point FFT of 8192 acquisition samples of a loudspeaker in an ordinary domestic living room. The curve is unsmoothed and clearly shows the effects of reflections which cause many peaks and dips. Resolution is 7.4Hz.

The whole 8192 point FFT of 8192 samples, but this time smoothed into 1/3 octave. Major dips and peaks are ironed out to show general response trend.



Samsung 286 machine a full-bandwidth waterfall takes fractionally over a minute due to the large number of computations required. But this can hardly be thought of as lengthy.

Time-domain responses and frequency-domain responses can both be stored. To avoid building up large lists of files I found it convenient to save just the whole time-domain response – from which all the other curves and measurements are derived – and perhaps one frequency-domain curve.



FFT of first of impulse with all room reflections removed. Frequency resolution is 330Hz, so low frequencies have been excluded from graph, printed as zoomed by cursors. This is the pseudo-anechoic response and is not smoothed in any way.

Bode plot of woofer unit showing amplitude and phase against frequency. Note the inaccuracy at low frequencies due to insufficient samples being taken at acquisition.

At a later date the time response can be recalled from memory and the various responses, phase plots, etc re-computed.

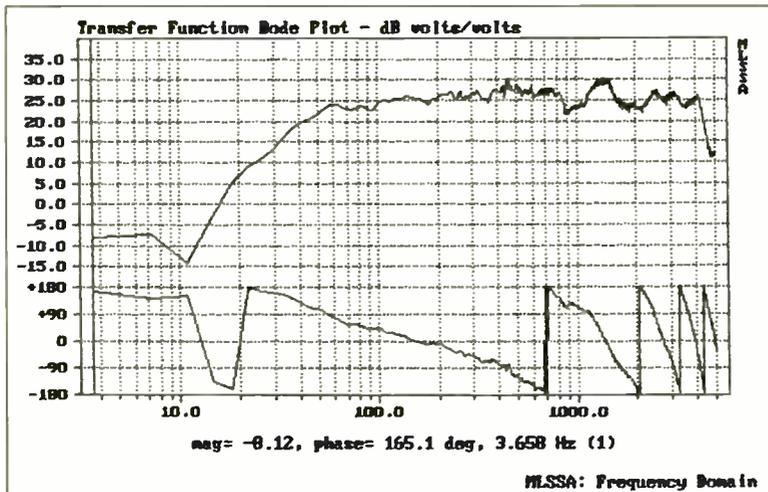
Macros allow measurements to be achieved automatically – particularly handy for repeated and tedious operations, such as polar response measurements, or perhaps measurements of vibration at different points on a loudspeaker panel.

For acousticians, Melissa's room measuring facilities will prove invaluable. By filtering Schroeder sound decay curves at various frequencies and selecting portions of the decay curves with the cursor, the RT 60 figures and early decay times can be presented. The only tedious aspect is the repetition, but it must still be quicker than any other way.

Even so if the effort proves too much, a macro can action the computations for different octave bands and print the results for you. Whichever way is chosen, just one acoustic measurement is required, with the rest of the work left to Melissa.

Keep an eye on printing

Once successfully up and running, I had no significant problems. First version of the software, 5.26, worked



Promise of Version 7

Version 7 is now on the way and is expected to include several refinements.

Of particular interest to loudspeaker designers is inclusion of Thiel Small parameter measurements using a complex curve fit algorithm. Because the algorithm does not rely on just three points on the impedance curve, it is claimed to be much more accurate than traditional techniques.

Version 7 should allow greater flexibility with overlays and provide an increased range of mathematical functions.

Double integration should allow acceleration, velocity and displacement to be viewed from an accelerometer input and there will also be enhancements to printer, file management and file exporting. To improve the available ram on 386 and 386SX computers, 386MAX will be bundled with version 7.

fine, though sometimes the display would "throw a wobbler", indicating unfamiliar numbers which would clear at the next command. Latest version 6 software, which includes useful features like sound pressure level measurements, was perfect from the outset and has caused no problems. The only minor niggle occurs when I occasionally try to print while the printer has run out of paper or is off line – the system locks up completely and refuses to respond to commands until the printer is brought on-line.

The reason is apparently because version 6 does not sense that the printer is not ready and just keeps on trying to print – a little foible which is to be cured in version 7. I am told (see box).

For printing I use the excellent little Kodak Diconix 150-plus portable ink-jet printer with the Samsung. It is light and compact and has a quite sharp print quality (curves in this feature have all been printed on ordinary paper on the 150-plus).

I have also used an HP Laserjet III without problems, apart from the time it takes to construct the image for the graphs; printing is much quicker on a dot-matrix or ink-jet printer.

Melissa is also compatible with the HPGL graphics interface.

Invaluable for loudspeaker design

I found Melissa to be a powerful tool for loudspeaker design work. It is especially useful for investigating hard-to-trace problems such as frequency response irregularities from tweeter horn resonances and tracking down effects due to grille frames and cabinet diffraction.

High-frequency mid-range-to-tweeter crossover work is also much easier without the clutter introduced by the room and this means that the microphone can be positioned at one metre, or further away, with Melissa still able to show how the loudspeaker is behaving.

The waterfalls are useful for indicating possible sources of audible coloration, though they need careful interpretation.

Where Melissa is not markedly better in an ordinary room than swept sine-wave techniques is at low frequencies. Here, because it is not possible to cut out reflections and have fine resolution, close microphone placement is still required to reduce the effect of the room (using Melissa in an anechoic room is a possible solution and I know of at least one manufacturer who does this).

A narrow acquisition bandwidth (say 5kHz) and a large FFT (4096 points) is required for an accurate low-frequency curve (3.66Hz resolution). Processing might be

expected to take longer than the wide-bandwidth curves, but Melissa produces a frequency-response curve in just under a minute.

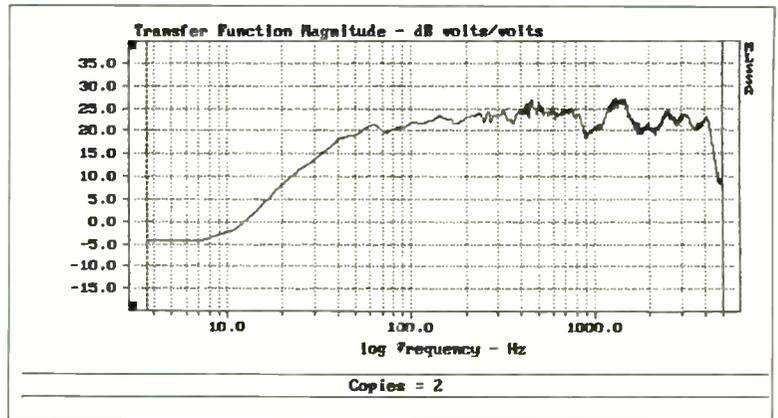
Pre-averaging can usefully be applied in these low frequency tests, helping the package to ignore any low-frequency background noise which can introduce inaccuracies. With pre-averaging and fine resolution, the Melissa curve is actually less cluttered by background noise than in-room sine-wave curves and in my view easier to interpret – provided the operator sets the acquisition length so as to achieve a narrow resolution.

With all measurements, the best approach is to set the acquisition to the same number of samples as the FFT. That way the set-up screen shows precisely the resolution that can be expected.

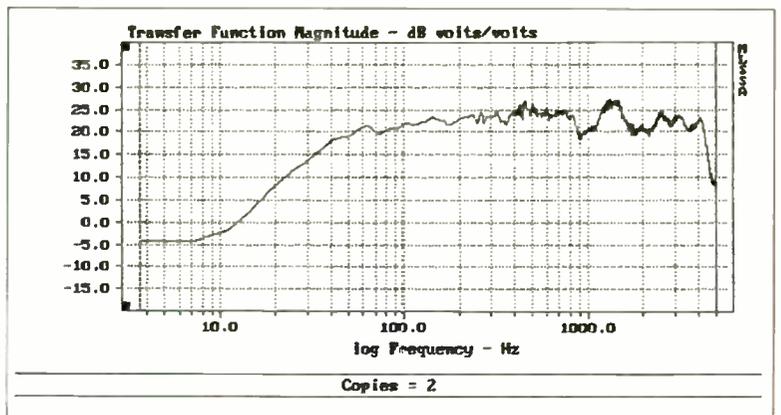
Version 6 has proved invaluable to me in loudspeaker design. But one more important feature is the upgradability of new software. As a result I am now eagerly awaiting version 7 with a particular eye on its Thiel Small parameter measuring abilities.

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5. LR Fincham. "Refinements in the Impulse Testing of



Low-frequency response taken with 5kHz bandwidth and 4096 points acquisition, giving a resolution of 3.66Hz. This was taken with the microphone at 12cm from the woofer and shows the response clearly down to about 10Hz.



Group delay for woofer in room with microphone at 12cm.

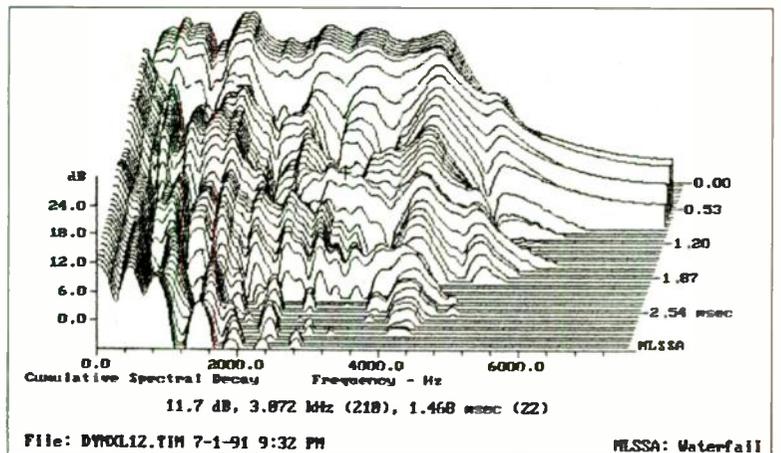
Melissa capabilities

Melissa can display the step response, frequency response, phase response, Bode and Nyquist plots, energy time curves, Schroeder reverberant decay curves and cumulative energy. It can measure impedance (both modulus and phase) and generate 3-D waterfalls, otherwise known as cumulative spectral decay graphs (there is also a variation on this known as the Wigner distribution). Early/late reflection ratios and reverb/direct ratio can be measured for acoustics work, and another function, known as coherence, allows errors introduced by the loudspeaker to be quantified. The function is a form of highly analytical distortion plot taken over a full bandwidth. But to make use of this facility the loudspeaker must be measured in an anechoic room – or well away from reflections which ruin the measurement.

Melissa can also measure accurate sound pressure level by referring to a library of microphone sensitivities, entered by the user.

A reference curve can be stored and compared to others, computing a difference curve, so that small changes introduced in, say, a crossover, can be accurately measured. It can also over-lay several curves on one screen for visual comparison. There are also numerous statistical computations which can be applied to the test results.

During system set-up, any inaccuracies introduced by the power amplifier etc, can be taken into account by storing the frequency and phase information about the amplifier link as a reference, which is subsequently automatically subtracted from the measurements. Also measurable are minimum and excess phase. The STI and RASTI speech intelligibility tests are also included. Programmable filters are included and these can be used to isolate reverberant decay within any octave or 1/3 octave band. Harmonic distortion can be measured



Cumulative decay spectra of loudspeaker in sealed box, showing the decay in sound output after the "stimulus" has stopped. Plotted with a linear frequency axis.

- Loudspeakers". *JAES*, Vol. 33, No 3, pp. 133-140, 1985, March.
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10. H Moller and C Thompson. "Electroacoustic Free-Field Measurements in Ordinary Rooms, Using Gating Techniques". *Bruel and Kjaer Application Notes*, 15-107.

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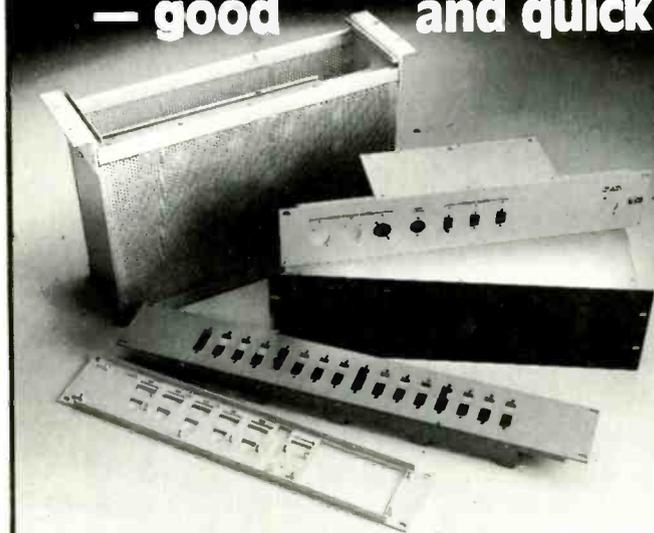
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THE CRUNCH FOR DSP CARDS ?

DSP power need no longer be limited to signal processing applications – if a new C compiler proves its worth.

Allen Brown sums up XCX.

Principal platform for hosting digital signal processor chips is the PC expansion card. Originally the PC was seen as a low cost development system for DSP chips with software tools (C compiler, a cross assembler, linker and simulator) running under ms-dos.

Compiled code was down-loaded to the expansion card to run in real-time if necessary. So the role of the PC was limited to a development platform only, but represented an attractive entry-level alternative to chip-specific development systems.

Many manufacturers produce expansion cards hosting DSP chips, with applications largely confined (or limited) to signal processing needs – an annoying restriction considering the computational power of DSP chips.

But it was inevitable, recognising that DSP chips are potent number crunchers, that moves would be made to make expansion cards with DSP chips more accessible to non-signal processing requirements.

Now Rich Software (distributed in the UK by Bores Signal Processing) has issued XCX extended C compiler. The software package enables C source code with standard I/O and graphics instructions to be compiled and executed on expansion cards with an AT&T DSP32(C) chip.

By linking run-time libraries to the compiled C code, Rich has enabled the DSP32(C) to perform computational aspects of the code, with I/O data exchanged with

the PC's CPU, accessing the PC's bios. Computational code written for Microsoft C, Quick C or Borland C compilers can be compiled for the DSP32(C) chip, targeting the DSP32(C) and not to the PC's CPU.

A marked upgrade in performance results. To demonstrate the improvement a short routine written in C for calculating a million square roots was compiled using XCX and down-loaded to a DSP32C on an LSI expansion card. It took seven seconds to complete.

The same piece of code, compiled with Microsoft Quick C, running on the PC's 20MHz 80386 with 80387 coprocessor, took 70s to complete – an order of magnitude slower.

The engineer or scientist who frequently refers to *C Numerical Recipes* (Cambridge University Press 1988) will find XCX a real joy as it also contains additional C instructions for manipulating matrices – an area where ansi C is particularly weak.

Manufacturers (Table 1) of expansion cards with the AT&T DSP32(C) may find a new customer base for their products providing they can produce cards with adequate memory and fast data transfer without the clutter of analogue I/O.

Rich Software also produces a similar Pascal compiler, though effort may have been better spent if attention had been focused on C compilers for other floating point DSP chips such as the TMS320C30. ■

System Requirements

Expansion Card with either AT&T DSP32 or DSP32C chip.
PC with expansion bus which matches card.
AT&T DSP32 C compiler, cross assembler and linker.

Availability

The XCX compiler (£300) and expansion cards listed in Table 1 are available from Bores Signal Processing, 39 Hawkswell Close, Woking, Surrey, GU21 3RS. Tel: 0483 740138.

Table 1. PC Expansion Card Hosting the AT&T DSP32(C).

Product code	Memory (bytes)	Analogue I/O	Price	Maker
ZPB32	64K (DSP32)	DSPlay serial i/f	£980	BB
XN1-AO	64K (DSP32)	buffered serial i/f	£700	CAC
ZPB32-HS	64K (DSP32)	DSPlay serial i/f	£1470	BB
XN1-BO	64K (DSP32)	8 bit, 8kHz codec	£650	CAC
XC4-ax	64K-256K	buffered serial i/f	£800-1000	CAC
PC-32C	64K-256K zero w/s	DSPport interface	£1200-1500	Ariel
ZPB34	64K-576K two w/s	DSPlay serial i/f	£1960-4900	BB
AC5-ax	64K-256K zero w/s	CAC daughter boards	£1000-1200	CAC
PC/DSP32C 1.2	two /s	DSPLink interface	£1400	LSI
V32C/256	128K-256K one w/s	DSPLink interface	£1400-1700	SMIS
PC-32M	256K-1.25M zero w/s	DSPport interface	£1800-3300	Ariel
AC5-ax-by 64K-1.25M	none one u/s	£1500-2200	CAC	
V32C/85	1.25M-8.25M seven w/s	DSPLink interface	£3200-4400	SMIS
DT2878	2-4M seven w/s	DT-Connect interface	£5000-6500	DT
ARIEL 32C 64K-256K	16 bit stereo 100kHz zero w/s	£2700-3000	Ariel	
AC5-ax-J	64K-1.25M one w/s	16 bit stereo 50kHz	£1800-3500	CAC
PCS/DSP32C	192K two w/s	16 bit stereo 200kHz	£2000	LSI

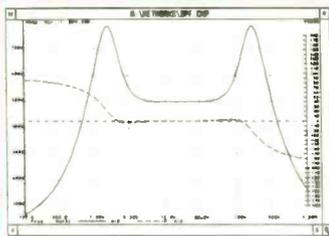
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- Module 2 - DC quiescent analysis ● Module 4 - Fourier analysis



Impedance sweep

2 DC Quiescent analysis

SPICE•AGE analyses DC voltages in any network and is useful, for example, for setting transistor bias. Non-linear components such as transistors and diodes are catered for. (The disk library of network models contains many commonly-used components - see below). This type of analysis is ideal for confirming bias conditions and establishing clipping margin prior to performing a transient analysis. Tabular results are given for each node: the reference node is user-selectable.

Node	DC Volt	Node	DC Volt	Node	DC Volt
1	0.0000	4	0.2711	7	2.7000
3	1.4161	6	0.2711	5	7.6250
4	1.6161	7	0.2711		

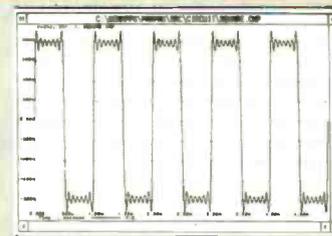
DC conditions within amplifier circuit

1 Frequency response

SPICE•AGE provides a clever hidden benefit. It first solves for circuit quiescence and only when the operating point is established does it release the correct small-signal results. This essential concept is featured in all Those Engineers' software. Numerical and graphical (log & lin) impedance, gain and phase results can be generated. A 'probe node' feature allows the output nodes to be changed. Output may be either dB or volts; the zero dB reference can be defined in six different ways.

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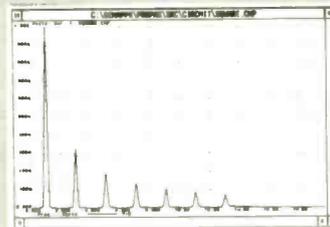
Square wave synthesis (transient analysis)

3 Transient analysis

The transient response arising from a wide range of inputs can be examined. 7 types of excitation are offered (impulse, sine wave, step, triangle, ramp, square, and pulse train); the parameters of each are user-definable. Reactive components may be pre-charged to steady-state condition. Up to 13 voltage generators and current generators may be connected. Sweep time is adjustable. Up to 4 probe nodes are allowed, and simultaneous plots permit easy comparison of results.

4 Fourier analyses now with Hanning window option

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Z80A DMA	0.90	0.65	2764A-25	1.60	1.20
Z80A (CMOS) CPU	1.20	0.90	27C64-15	1.65	1.35
Z80B (CMOS) CTC	0.70	0.45	27C128-25	1.75	1.45
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1489	0.14	0.12	27256-25	1.80	1.40
ILQ-74	1.20	0.85	27C256-200	1.90	1.55
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6522AP	2.20	1.50	41C1000AP-80	4.10	3.25
6551	2.00	1.40	74LS04	0.10	0.07
65C21P2	2.80	2.40	74LS138	0.17	0.12
8031	1.90	1.40	74LS273	0.21	0.16
8251A	1.10	0.75	74LS368	0.14	0.10
8255-5	1.20	0.90	74LS373	0.20	0.14
8259AC	1.00	0.70	74LS374	0.20	0.14
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74LS02	0.10	0.07	74HCT373	0.18	0.12

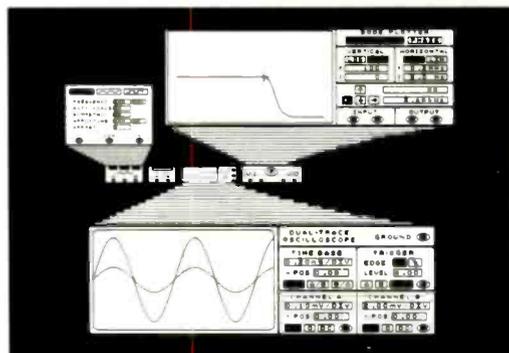
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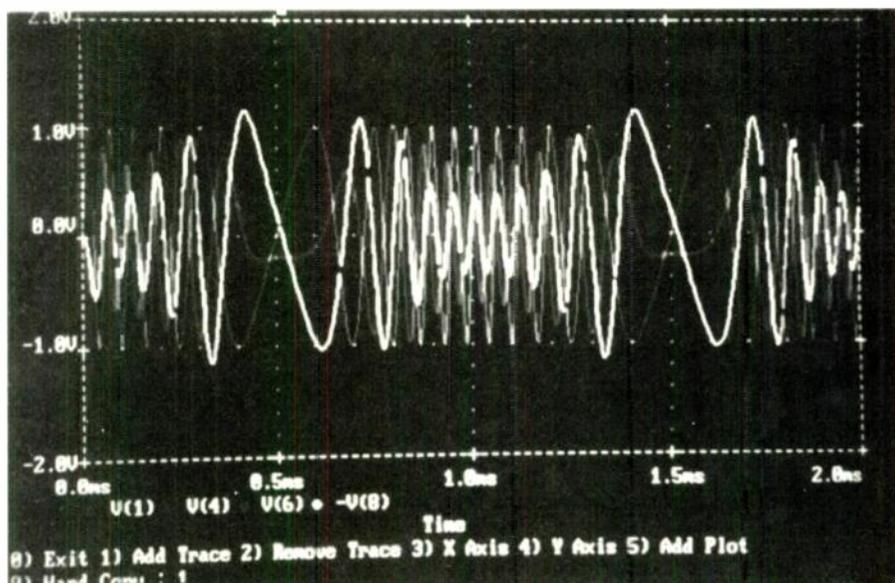
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CIRCLE NO. 112 ON REPLY CARD

ADDING SPICE TO TECHNOLOGY

£30 and an IBM PC are enough to allow anyone to experiment with a wide range of electronic devices without having to connect even a single wire. Paul Stewart explains how to set about it.



A PC version of Spice (Microsim's simulation program with integrated circuit emphasis) now provides the user with a hands-off means of experimentation. Helped by a book called "Spice, a guide to circuit simulation & analysis using Pspice" by P.W.Tuinenga and published by Prentice Hall, he can gain access to a variety of electronic devices - from resistors and coils to transmission lines and quartz crystals - without so much as the need to connect a wire. The response of circuits to a variety of programmed stimuli can be monitored using a simulated oscilloscope.

This minimalist approach is aimed at the student; Microsim also offers evaluation and production versions. The evaluation package offers menu-driven software and comes with a complete 450 page document describing in much greater detail than Tuinenga's book all

of the routines, parameters and options of the full Pspice package. Both this and the student version have a small library of device parameters or characteristics. The more expensive full production version has an extensive library of devices, including over 3000 analogue and 1200 digital devices.

Although only a rather small volume of device data is available in the student version, Tuinenga shows in his book how model parameters can be included for devices not covered by the library (see also the book by Antognietti and Massabrosi).

One important thing to remember with a software circuit simulator is that you cannot blow up a device: the computer will still give answers even if you try to drive a 100mA transistor with 10A. Make sure then that, before building your simulated circuit

Analogue simulation waveforms using the PSpice analogue simulator from ARS Microsystems.

with real components, each of the various components is working within its power limit.

Pspice capabilities

Any competent engineer will be able to calculate mathematically the frequency at which an oscillator circuit will oscillate, provided that the amplitudes of the voltages of the waveforms generated are small in every part of the circuit. He may also be able to estimate the output voltages of such a circuit and even, with extreme difficulty, to assess the true frequency of oscillation, allowing for the existence of large amplitude swings.

In a complex circuit, the mathematics

becomes too complicated; over the last thirty years engineers have therefore resorted to the use of the computer, even for circuits

Component types

Any electrical circuit may be described in terms of nodes or points of connection between the two different types of component from which it is made up. Passive devices such as resistors, capacitors and coils are components that passively transfer or dissipate energy without themselves being the source of it. Active devices such as diodes and transistors may have external bias energy applied. Part of this energy is used actively to increase the energy or modify the nature of a required signal.

In general, passive devices are rather easier to deal with because there is a simple one-to-one correspondence between the current flowing through them and the voltage developed across them. For example, the current through a resistor will double if the voltage applied to it is doubled, although this is not true for diodes and transistors, which are non-linear. This non-linear behaviour of active devices is what makes them so difficult to analyse and where a software package like Pspice comes into its own.

consisting entirely of passive components - for example, filters with twenty components. Although Pspice can cope with all this, it must be said that there can be no substitute for good design and flashes of inspiration!

The Pspice software simulator is controlled by a simple language with instructions in two broad categories: control statements and devices. Control statements instruct the computer to perform various

types of analysis and produce output data in different formats: graphical and tabular. The devices section of the language is used to describe the types of device in a circuit and the connections made between them. The many control statements include instructions to calculate the DC voltages in a circuit, its frequency response and transient response to a variety of applied voltages such as sine, pulse and FM.

The following examples demonstrate some of the package's many facilities and give a better appreciation of the way in which the computer is instructed to perform various tasks.

DC calculations

At the simplest level of any circuit calculation is the determination of the currents and voltages resulting from the application of steady DC voltages.

In a simple circuit consisting of two series resistors of 1 and 3Ω connected across a 1V DC supply, the following table shows the input file which describes the circuit in Pspice language.

```
potential divider circuit
V1 1 0 1V
R1 1 2 1Ω
R2 2 0 3Ω
.end
```

The first line of any Pspice program must be a string of symbols which serves to title the program; it has no significance as an instruction. The second line indicates that a steady voltage source of 1V is connected between points labelled 1 and 0 with node 1 at +1V, relative to node 0. Every Pspice program must be terminated with an .end. Any line of a Pspice program that starts with an asterisk is ignored. It resembles an REM statement in Basic, and is used to insert remarks that make the program more readable.

If this program of instructions is held in a file called EXAMPLE.CIR, when the instruction pspice EXAMPLE.CIR is typed into the com-

puter the program will be executed. After a short time another file, EXAMPLE.OUT, will be produced, part of which will look like this:

NODE	VOLTAGE	NODE	VOLTAGE
1)	1.0000	2)	.750

This table gives the voltages at various nodes relative to the 0 reference node; hence there is 1V between node 1 and 0 as one might expect since that is the voltage applied to the circuit. The other two figures indicate that between nodes 2 and 0 there is a voltage of 0.750V.

In fact this circuit is nothing more than a potential divider with 3/4 of the total series resistance between terminals 2 and 0. This trivial example serves to show the basic structure of a program.

One point that should be noted is that computers fail if any attempt is made to divide a number by zero. This has certain implications for the execution of pspice in DC analysis of circuits with inductors and capacitors.

AC calculations

In circuit analysis, the frequency response of a circuit such as a filter or amplifier often needs to be determined. **Figure.1** shows a 50Ω 5-element low-pass filter with a design cut-off frequency of 1MHz. It consists of two inductors, I_1 and I_2 with values 10.73μH and connected between nodes 1 and 2 and 2

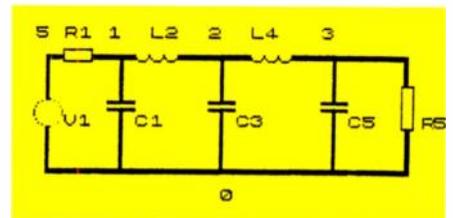
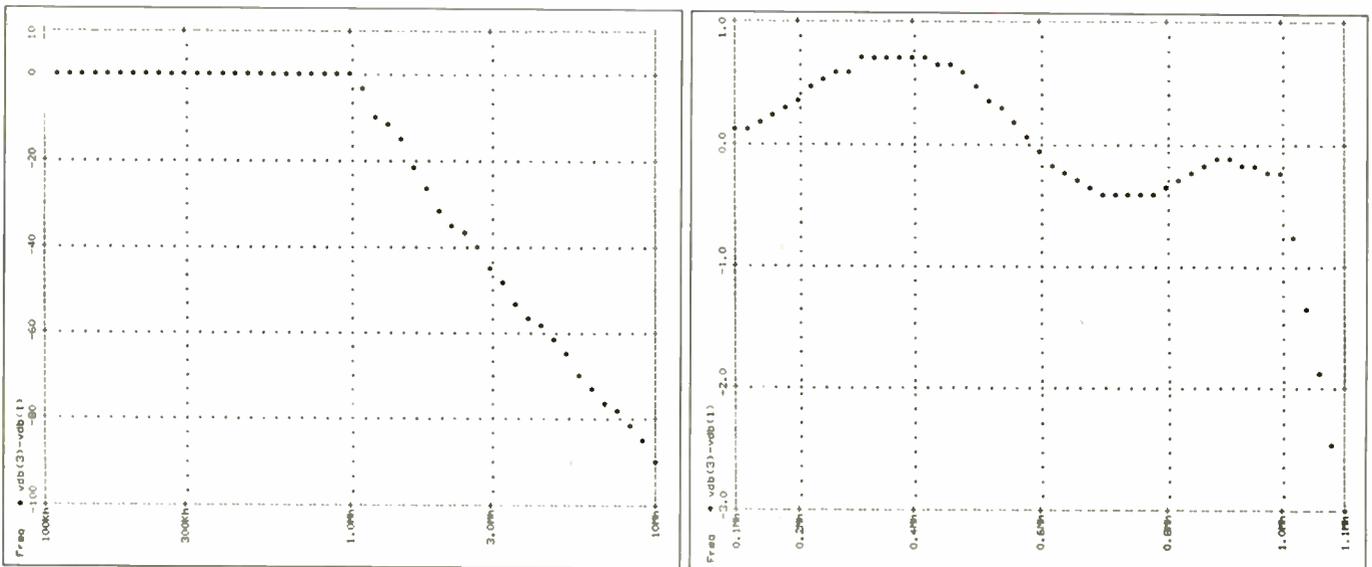


Fig. 1. 1MHz lowpass filter network

The left hand plot shows the frequency response of the filter network with the associated passband ripple indicated on the right



and 3; the capacitors C_1 , C_2 and C_3 are connected between ground, node 0, and nodes 1, 2 and 3, respectively with $C_1=C_2=3000\text{pF}$ and $C_3=5600\text{pF}$. The filter is terminated with its characteristic impedance of $R_5=50\Omega$ and fed by a signal generator V_1 with a source impedance that is also 50Ω . The corresponding Pspice program is shown below:

```
r.f low-pass filter
v1 5 0 ac 1
r1 5 1 50Ω
c1 1 0 3000pF
l2 1 2 10.73μH
c3 2 0 5600pF
i4 2 3 10.73μH
c5 3 0 3000pF
r5 3 0 50Ω
.ac dec 20 .1e6hz 100e6hz
.probe.end
```

Only three of these lines require explanation; line 2: $v_1\ 5\ 0\ ac\ 1$ indicates that an AC voltage of nominally 1V is applied between nodes 5 and 0; line 10: $.ac\ dec\ 20\ .1e6hz\ 100e6hz$ indicates that the voltage source v_1 applied to the filter is to be swept through 20 different frequencies in decades from 0.1 to 100MHz; the symbol $e6$ is used to indicate 10^6 as a multiplying factor (the symbol Meg may also be used); line 11: $.probe$ instructs the computer to store all current and voltage values at and through each node in a file called PROBE.DAT.

When the program ends, you should type $.PROBE$ into the computer. A menu will appear, offering you a variety of choices of graphical presentation of the computed data. As the name implies, the action of PROBE is to simulate an oscilloscope probe, providing a graphical view of the voltages and currents at any point in the circuit.

In Pspice talk, this $.ac$ type of analysis gives what is called the small-signal steady-state response to the input; the number 1 at the end of line 2 does not mean 1V but is simply an arbitrary defining constant for V. The analysis assumes that the input signal is very small so that, if components such as transistors are included, they are not driven far from the DC bias conditions.

Of course, the filter circuit described above does not contain non-linear devices. Small-signal analysis is appropriate when the frequency response of an input RF receiver amplifier is being determined, but not for the response of an RF power amplifier of a transmitter where the input signal levels are very high; for example in class C mode.

Considerably higher volumes of data may be accessed through the use of PROBE than is discussed here, including the delay of a pulse of CW through the circuit and the phase of the output sine wave relative to that of the input.

Transient analysis

Transient analysis mode is particularly interesting. All electronic circuits are subject to transient behaviour, but whether this is important depends on the time the circuit

takes to stabilise compared with the period over which it is handling a signal. For example, if a short burst of audio tone is passed through a high Q band-pass audio filter, the output of the filter may have an unacceptable ring which can be so long as to run into the next burst of tone; this is a well-known problem in CW filtering of high speed Morse signals.

The transient analysis mode in Pspice has another important feature: it allows the effects of large signals in a circuit containing non-linear elements like diodes and transistors to be determined. As we all know, over-driving an RF power amplifier produces harmonics. One simple example of transient analysis using Pspice (outlined below) forms the basis of Time Domain Reflectometry.

Figure 2a shows a transmission line of 50Ω impedance; to the input of the line is connected a $50\Omega/1\text{V}$ pulse generator; the other end of the transmission line is shorted. If the pulse generator voltage "vpulse" rises from 0V to 1V at a time 10ns from the time origin 0 and is then held at that voltage indefinitely, what is the voltage at the input terminal to the transmission line at different times?

In fact what happens is that the pulse takes 10ns to travel down the line to the short, where it is inverted and reflected back

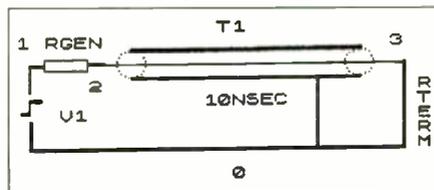


Fig. 2a. Short-circuited transmission line model

towards the pulse generator. This cancels the on-coming 1V from the generator, leaving 0V in its wake. 20ns after switch-on, the reflected signal cancels the on-coming wave completely at the input to the transmission line; from then on, there is no voltage across the line's input terminals although the 1V is sustained at the input to the 50Ω resistor.

This circuit is simulated using the Pspice program below:

```
pulsed transmission line
t1 2 0 3 0 Z0=50Ω td=10nsec
rgen 1 2 50Ω
rterm 3 0 .0001Ω
v1 1 0 pulse(0v 1v 5nsec 0nsec 0nsec 50nsec
500nsec)
.tran .05nsec 30nsec
.probe
.end
```

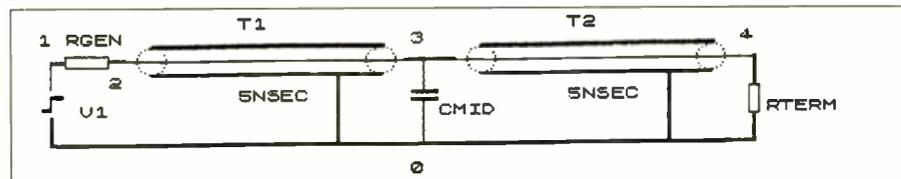


Fig. 2b. Transmission line model. The capacitance in the middle represents the effect of a drawing pin compressing the cable

Four of these lines need some explanation: line 2: $t_1\ 2\ 0\ 3\ 0\ Z_0=50\Omega\ td=10\text{nsec}$. Any device beginning with a t indicates a transmission line; the input is connected between nodes 2 and 0 and the output appears between nodes 3 and 0; $Z_0=50\Omega$ refers to the line's characteristic impedance and $td=10\text{nsec}$ is the delay length: 10 units of ns ($1\text{ns}=10^{-9}\text{s}$).

Line 4: $rterm\ 3\ 0\ .0001\Omega$. The very low value of $rterm$ ($.0001\Omega$) has been given a value close to zero without actually making it zero since computers fail to compute with zeros; this simulates a short circuit at the output end of the line t_1 .

Line 5: $v_1\ 1\ 0\ pulse(0v\ 1v\ 5\text{nsec}\ 0\text{nsec}\ 0\text{nsec}\ 500\text{nsec}\ 500\text{nsec})$ this statement sets the voltage source v_1 to a pulse of 1V which switches from 0V at time=0 to 1V at time=5ns, with rise and fall times of 0s and has a 500ns period with the voltage being developed across nodes 1 and 0; Line 6: $.tran\ .05\text{nsec}\ 30\text{nsec}$. This line instructs the computer to calculate the voltages and currents in the circuit over a 30ns period and to record them at .05ns intervals.

Addition of the $.PROBE$ statement produces a file PROBE.DAT which, after the execution of the above program, can be accessed by typing $probe$ as before.

Now consider two minor modifications to this circuit. Place a 5pF capacitor half way along the transmission line and across it and replace the short with a 50Ω resistor at the end of the line. This simulates the effect on a matched coaxial line which is fixed too hard into a wall with a U-shaped pin that compresses the cable, thereby increasing its capacitance locally. The circuit is shown in Fig. 2b.

If we apply the same pulse to the line and ask for the transient response, the Pspice program becomes:

```
defective transmission line pulsed
t1 2 0 3 0 Z0=50Ω td=5nsec
rgen 1 2 50Ω
cmid 3 0 5pF
t2 3 0 4 0 Z0=50Ω td=5nsec
rterm 4 0 50Ω
v1 1 0 pulse(0v 1v 5nsec 0nsec 0nsec 50nsec
500nsec)
.tran .05nsec 30nsec
.probe
.end
```

The PROBE facility can again be invoked to inspect the line voltages. With the line voltages displayed by PROBE in low time resolution (see Fig. 2c), because the input voltage pulse $V(1)$ takes 5ns to reach the capacitor, the effect of the capacitor is not felt until after that time.

Fig. 2c. Transmission line voltages vs time (low resolution)

When the leading edge of the pulse strikes the capacitor, the sudden change in the capacitor potential makes the capacitor behave momentarily like a short circuit; the capacitor then proceeds to charge up to a steady voltage with a time constant of 0.125ns. This is half the time constant formed by 50Ω and a capacitor of 5pF. 10ns after the pulse has switched on at the input end, the information is received at the far end.

What of the signal reflected back to the generator? There are two possible reflections, one from the capacitor and the other from the termination at the end of the line t_2 . The latter does not occur because, of course, the line is perfectly matched to the load.

The voltage that appears at the input end, node 2, is then the effect of the input voltage from the pulse generator and the signal reflected from the capacitor. 10ns after the pulse is switched on, the signal which is reflected back from the capacitor has had time to make its effect felt on the input, node 2. In the first instance it produces an effective short similar to the previous example, so that the voltage drops to zero; this effect decays gradually to produce a steady distribution of voltages throughout the line with the input and output voltages both becoming 0.5V. **Figure.2d** shows the voltages at various points with a finer time resolution.

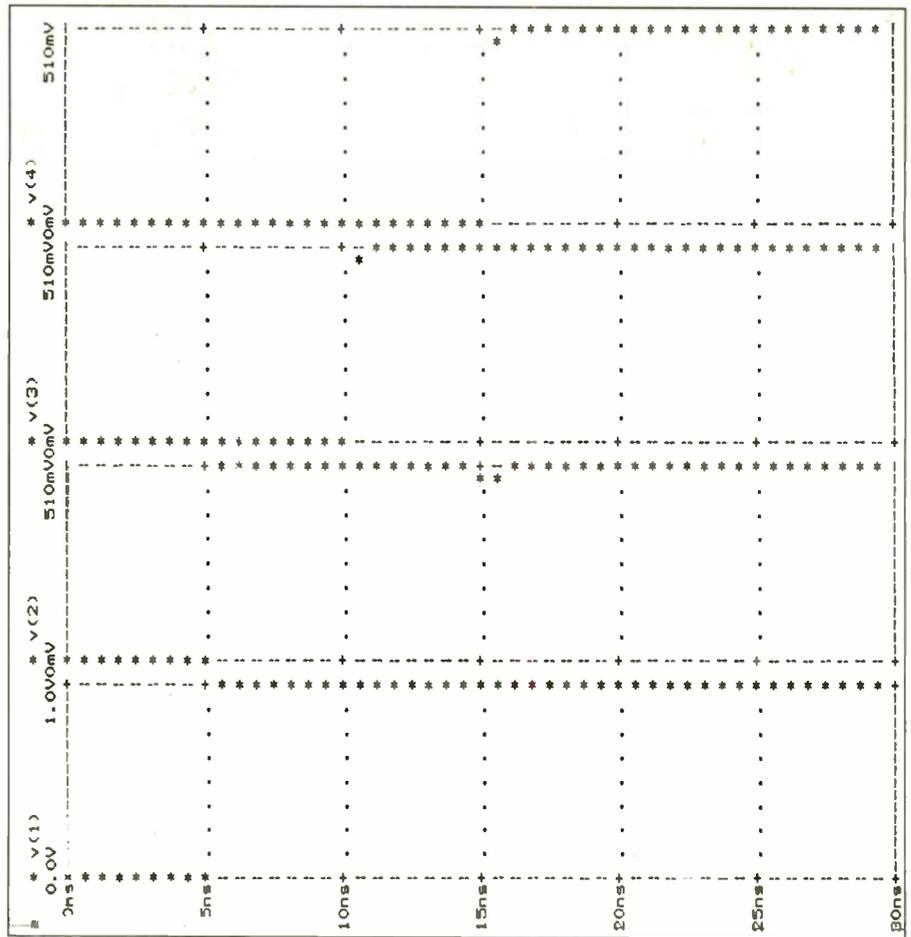


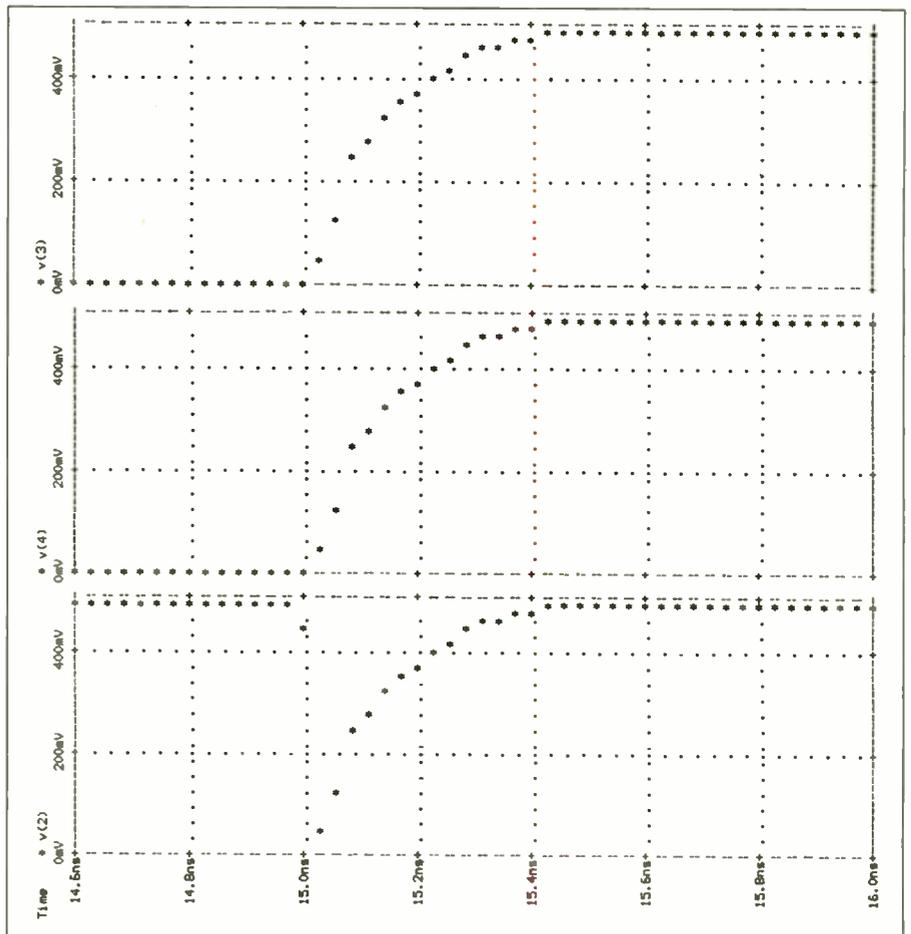
Fig. 2d. Transmission line voltages vs time (high resolution)

Other Pspice features

Since the 1987 student version was written, the codes of the evaluation and production versions have been updated. These two versions now include a powerful digital option that - amongst other features - enables TTL and discrete components to be interconnected. The PROBE may be invoked to give analogue voltages and a logic analyser display in terms of the 0s and 1s of various logic states as a function of time.

This facility necessitates the modelling of the I/O interfaces of TTL, cmos and ECL chips in analogue form as well as the various propagation delays from all of the internal components between the interfaces. Such models may be constructed either by the user or by invoking a digital library using a .LIB command, although this is not included in the student version.

Two other features available in evaluation and production versions are described under the heading Analogue Behavioural Modelling. It is possible, for example, to give the voltage current relation for a device in terms of a numerical table; such a facility is useful in modelling say a tunnel diode. Another aspect of this feature is its ability to write, in the form of a table, the frequency response of a filter which you wish to include in a larger circuit.



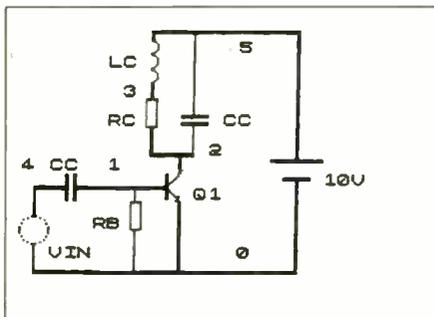


Fig. 3a (top) Transistor tripler model.

Fig. 3b (right) shows variations of the output voltage, $v(2)$ the collector current $ic(q1)$ together with that of the input voltage $v(4)$ for the last oscillation of the input voltage.

Fig. 3c displays the amplitudes of the various harmonics in the output voltage $v(2)$ at the collector, the largest of which is the third as required

As a final example of Pspice, consider the tripler circuit of Fig. 3. We shall apply a 2MHz sine wave of amplitude 0.8V between the base and emitter of a 2N2222 transistor. A 10V supply feeds the transistor via a parallel coil and capacitor – the latter two components being chosen to resonate at the third harmonic of 2MHz. The program simulating the transient response follows.

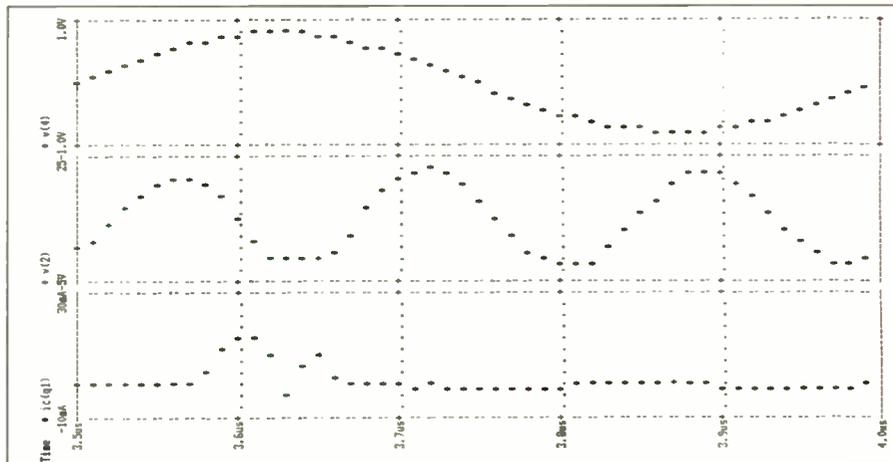
```
transistor frequency tripler
.options itl5=0
.lib
q1 2 1 0 Q2N2222
vsupply 5 0 10v
rb 1 0 1kohms
lc 5 3 10e-6
rc 3 2 7.5ohms
cc 5 2 70pF
cb 4 1 1nF
vin 4 0 sin(0 .8v 2meg 0 sec 0)
.tran .1e-6 4e-6 0 .01e-6
.four 2e6v(2)
.probe
.end
```

The resistor rc is chosen to give the $10\mu\text{H}$ coil lc a realistic Q of 50 at 6MHz. The device $q1$ is a transistor with nodes 2, 1, and 0 as collector, base and emitter respectively. The model type "2N2222" has parameters held in the library and invoked by the `.lib`

Software

Evaluation and production versions are available from ARS Microsystems, Doman Road, Camberley, Surrey, GU15 3DF.

The evaluation version includes Tuinenga's book, a 450 page manual covering a complete list of routines plus two 1.2MB high density disks. The software for both the student and evaluation versions may be freely copied; this is encouraged by Microsim Corporation.



```

..
.. DC COMPONENT = 9.991873E+00
..
.. HARMONIC FREQUENCY FOURIER NORMALIZED PHASE NORMALIZED
.. NO (HZ) COMPONENT COMPONENT (DEG) PHASE (DEG)
..
.. 1 2.000E+06 4.204E-01 1.000E+00 -8.411E+01 0.000E+00
.. 2 4.000E+06 1.239E+00 2.948E+00 -1.604E+02 -7.624E+01
.. 3 6.000E+06 1.086E+01 2.584E+01 -3.524E+01 4.887E+01
.. 4 8.000E+06 8.374E-01 1.992E+00 -1.196E+02 -3.551E+01
.. 5 1.000E+07 3.344E-01 7.956E-01 1.759E+02 2.600E+02
.. 6 1.200E+07 2.037E-01 4.845E-01 1.381E+02 2.222E+02
.. 7 1.400E+07 1.829E-01 4.350E-01 5.908E+01 1.432E+02
.. 8 1.600E+07 1.695E-01 4.031E-01 -1.315E+01 7.096E+01
.. 9 1.800E+07 1.750E-01 4.164E-01 -8.564E+01 -1.529E+00
..
.. TOTAL HARMONIC DISTORTION = 2.610554E+03 PERCENT
..

```

command on the second line.

In this program, the transient analysis proceeds for about four microseconds with data recorded every $0.1\mu\text{s}$. The purpose of the instruction "four..." is to perform a harmonic analysis on the output voltage of the tripler during last $0.5\mu\text{s}$ ($=1/2\text{MHz}$) of the transient analysis when, hopefully, a steady state has been reached. Fig. 3b shows variations of the output voltage, $v(2)$ the collector current $ic(q1)$ together with that of the input voltage $v(4)$ for the last oscillation of the input voltage.

Fig. 3c displays the amplitudes of the various harmonics in the output voltage $v(2)$ at the collector, the largest of which is the third as required.

Computer system requirements

The student version of Pspice will run on an IBM compatible PC or PS/2 based on the 8088, 80286 and 80386 microprocessors; it will also run on a Macintosh, but you should specify which. Both monochrome and colour monitors are supported.

While the student and evaluation versions will work without a maths co-processor, both will run about ten times faster if one is installed; the full production version does, however, require a co-processor. Software is supplied on two 5 in double-density double-sided disks for the student version and two high density disks for the evaluation version.

Pspice runs under MS-DOS 2.0+ with at least 512kB of RAM. The production version will also run on a variety of workstations. Apart from the production version, the capacity is limited to about 10 transistors or

25 nodes; the full version however is limited by the available RAM and has a typical capacity of 1000 resistors or about 100 transistors per 500kB of memory.

Which version?

This article has concentrated on the student version of Spice prepared by Microsim for the obvious reason that it is cheap, supported by a reasonably priced book and usable on a cheap computer. Apart from the other more elaborate versions mentioned, there are a number of other versions of Spice. Among these are Spice-Plus by Analogue Tools, Dspice by Daisy Systems, AllSpice by Intusoft, Z-Spice by Z-Tech and Spice-Age by Those Engineers. ■

Acknowledgements

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References

Semiconductor Device Modelling with SPICE, ed. P. Antognetti & G. Massobrio, pub. McGraw-Hill Book Co. (ISBN 0-07-002107-4), 1988.

See p6 for details on obtaining your free evaluation copy of Pspice...

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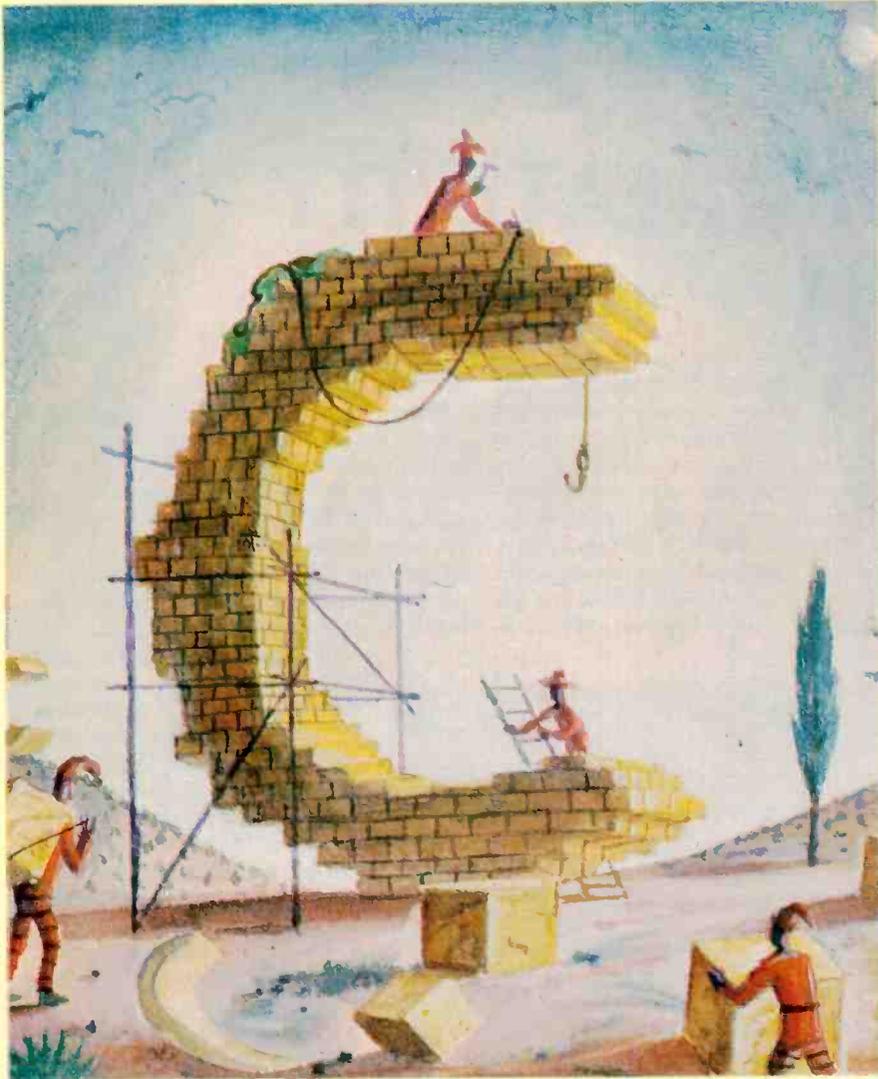
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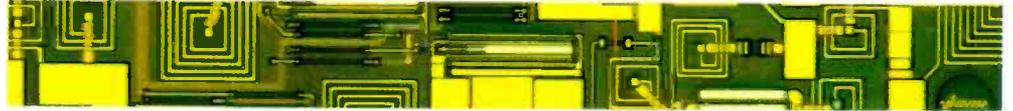
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INTEGRATED CREATIVITY

Ian Hickman experiments with the unusual SMM-2044 audio IC

Adding a component or two for which you have no immediate use to the end of your order is not as profligate as it might sound. Often the extra items can be used to avoid a "small order" surcharge, and so arrive, if not for free, then at least with a useful discount.

The resultant uncommitted stock items can come in very handy in an unforeseen application.

Sometimes an end-of-order component stays in stock for some time – until curiosity gets the better of me and I can't resist playing with it to find out what it can do. So it was with an SMM-2044, described by manufacturer PMI as a four-pole voltage-controlled filter/oscillator.

The device comes in a 16 pin plastic DIL package (Fig. 1). Input is applied to an npn long-tailed pair (LTP) whose standing current is set by the frequency control input, V_{fc} , applied to pin 13. Output of the LTP is applied to a series of four single pole low-pass stages. Cut-off frequency of each is controlled by the current called up by the exponentially controlled tail-current generator (common to all four stages) and the capacitor that is associated with the particular stage; eg between pins 12 and 14.

Output from the fourth voltage-controlled filter stage (VCF) drives a current output

stage – terminated to ground through (typically) a 3K3 resistor to give a voltage output or, if a larger low impedance output is desired, applied directly to the virtual earth of an inverting op-amp stage. Additionally, output from the fourth stage feeds another npn LTP whose standing current is also adjustable. A feedback loop is introduced by injecting a current into the Q control pin, pin 2, and has the effect of applying a replica of

the output back to the input of the first LTP.

Clearly Fig. 1 is somewhat diagrammatic, since it appears that the feedback is positive at DC – at least if there is no net inversion through the four VCFs – whereas the second LTP applies DC negative feedback (NFB). But what happens when no current is injected into pin 2, so that the second LTP is effectively non-existent and there is no feedback? Assume for the moment that all four

VCF capacitors have the same value, then at some frequency each VCF stage will contribute a 45° phase lag and an associated 3dB of attenuation. The result is a gradual transition from a flat frequency response at low frequencies; through -12dB at the cut-off frequency of this very non-optimum low-pass filter; to a stop-band attenuation increasing at 24dB per octave (Fig 2a). As the second LTP is progressively powered up by Q control, the NFB reduces gain through the device at low frequencies.

But at the frequency where each VCF stage contributes a 45°

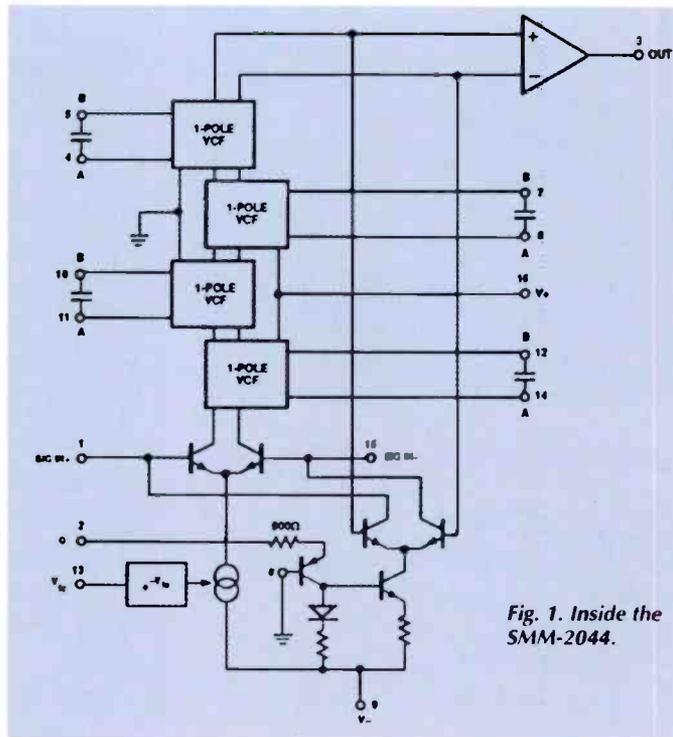
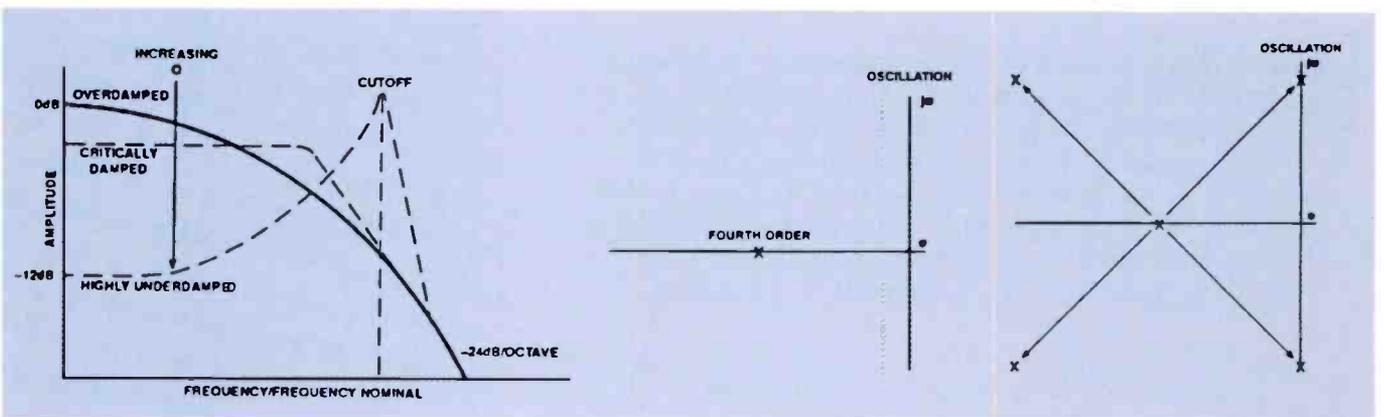


Fig. 1. Inside the SMM-2044.

Fig. 2a (left). Gradual transition in frequency response at low frequencies, through -12dB at cut-off frequency, to a stop-band attenuation increasing at 24dB/octave.

Fig. 2b (centre). Pole diagram. Fourth-order transfer function $Q=0V$.

Fig. 2c (right). Transfer function as Q increases.



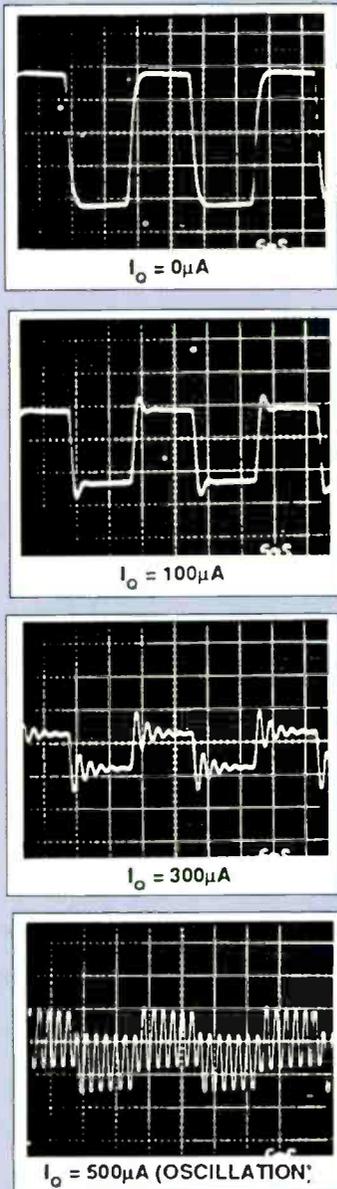


Fig. 3. Effect of applying a square wave to the circuit for different values of I_Q .

phase lag, total phase shift is 180° . The feedback has become positive and so the gain through the device will be enhanced. The four coincident poles (Fig. 2b) then migrate outwards (Fig. 2c).

If transconductance of the second LTP is increased then eventually the loop gain will exceed unity and oscillation will result, as two of the poles reach the $j\omega$ axis. A square wave applied to the circuit for various val-

ues of I_Q shows a reduction in amplitude of the square wave as Q is increased (Figs. 3a-d), top to bottom.

An interesting – and as far as I was concerned totally unforeseen – result appears when the Q control is set just short of oscillation. When frequency of the square wave is such that one of its harmonics coincides with the resonant frequency of the circuit, Fig. 3d results. At other frequencies waveforms such as Figs. 4a and 4b are seen; on one half cycle of the square wave, a harmonic is pretty well in phase with the natural frequency of the filter while on the other it is trying (and failing) to fit in an odd number of half cycles of the harmonic.

This explanation is rather simplistic but perhaps a knowledgeable reader will write in with a more exact description – preferably one not involving too much of the higher mathematics.

Possibly the effect is due to an unequal

Fig. 4. In one half-cycle of the square wave, harmonics are in phase with the natural frequency of the filter while on the other there is a failure to fit in an odd number of half cycles of the harmonic.

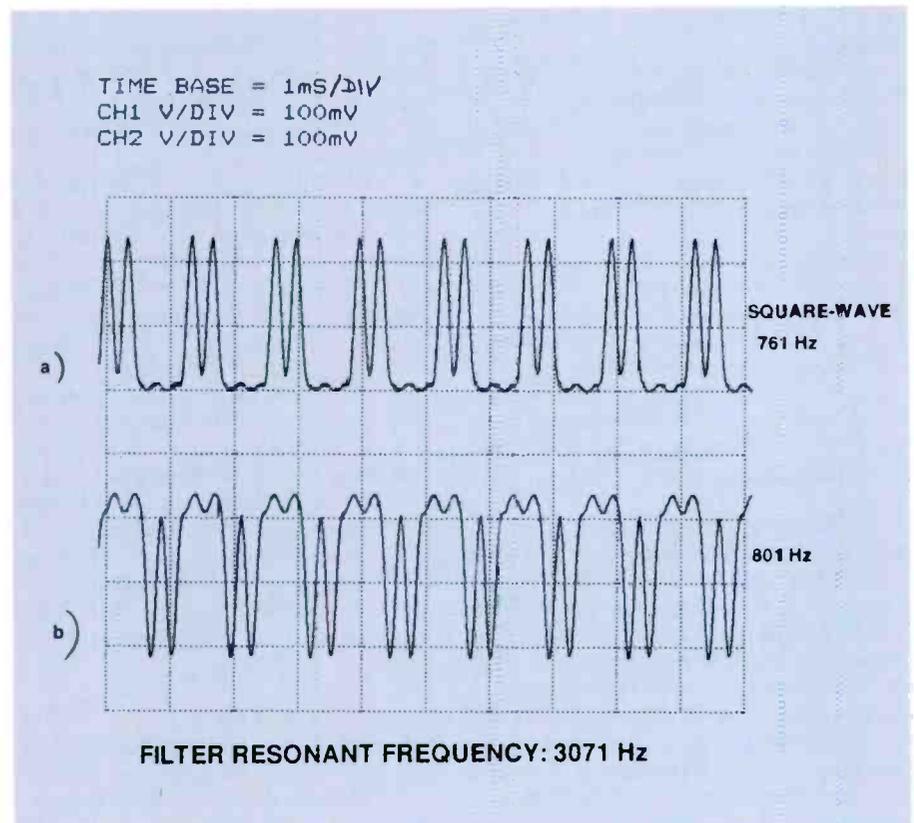
Uncommitted logic

Creating a stock of uncommitted components through adding the odd item to component orders can give a definite flexibility to problem solving.

A typical example arose recently when I was developing a small 12/24VDC to 240VAC inverter. The devices driving the transformer were the familiar TIP121s, driven straight from the outputs of a 5V CMOS source of 50Hz pulses derived from a 32768Hz crystal.

But they were groaning somewhat with the exertion, especially on a 12V supply where their saturation voltage was contributing embarrassingly to the circuit's poor regulation.

At that point I remembered I had bought in, on the end of an order, some BUZ10 mosfets. Their drain saturation resistance of only 0.08Ω cured the regulation problem at a stroke. They accepted the CMOS drive directly, and even had a pin-out making them drop-in replacements for the TIP121s! Problem solved – without any delay in procuring components. LH.



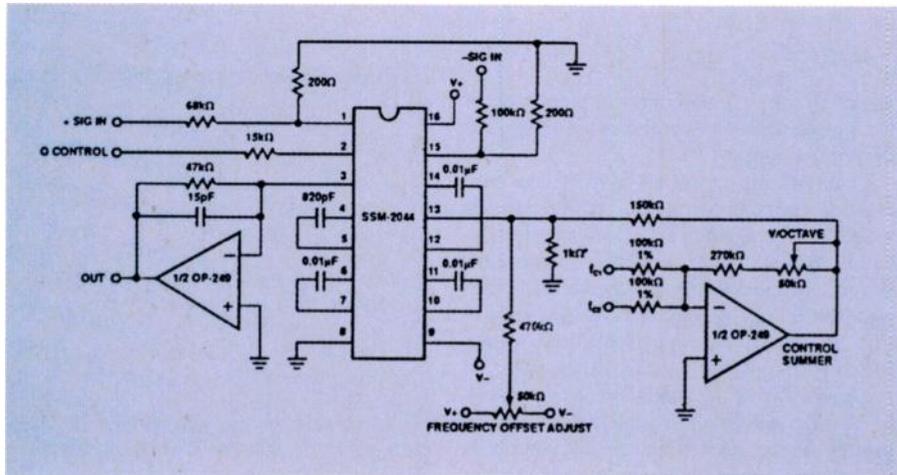
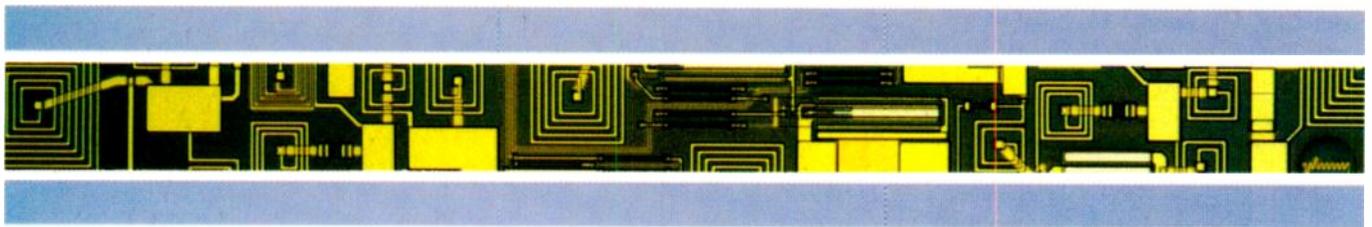


Fig. 5. Typical connection for breadboarding purposes, used as the basis for a programmable tone generator.

from the PMI Audio Handbook Volume 1, – the SSM-2120 dynamic range processor, the SSM-2100 log/antilog amplifier, etc.

Just one point worth noting; I found it useful to add 10µF decoupling capacitors, not shown in the recommended circuit diagram, from the V+ and V- supply rails to ground. This cured a tendency for a low-level 6MHz oscillation to appear at high Q settings. ■

mark/space ratio of the square wave, though I measured this as being a very respectable 49.5/50.5. The effect is still there even though the filter is not picking out a very high harmonic (Fig. 4).

Striking musical effects

Providing as it does independent control of Q and resonant frequency, the device can produce striking effects when applied to programme material such as music. A sample of the audio signal can be passed through the filter, modified, and then recombined with the original signal, either in phase or in antiphase.

Sweeping the resonant frequency of the filter up or down at different rates and Q settings can present novel effects, either manually or under program control from a computer, using D-to-A outputs from the latter to control both the centre frequency and Q.

A further possibility is to make filter parameters vary in sympathy with some aspect of the programme material itself, making envelope amplitude control the centre frequency or Q, for example.

But this versatile chip is not limited to filtering applications. By increasing Q up to the point of oscillation, it becomes a programmable tone generator.

Programmable tone generator

For application as a programmable tone generator, I used the recommended typical connection for breadboarding, Fig. 5. Note that one of the four capacitors is reduced to 820pF, leaving three coincident poles (Fig. 2b), but pushing the fourth one out by a factor of 12 along the $-\sigma$ axis. Oscillation sets in with around 500µA injected at pin 2, agreeing with the figure in the electrical characteristics Table of the data sheet, so I surmise that those figures apply to the cir-

cuit of Fig. 5, whereas Figs. 2, 3 and 4 apply to the case of four equal capacitors.

With +13.5V applied to the 15K Q control resistor at pin 2, output from the op-amp is 8V pk-pk, varying by less than 1dB over a tuning range of 3Hz to 45kHz. At 1kHz total harmonic distortion (THD) is 0.75% – hardly suitable as a low distortion oscillator when making THD measurements on other equipment, but more than adequate as a general purpose programmable tone generator. Reducing current into pin 2 gives 6V pk-pk output and distortion falls to 0.3%. But output at 45kHz is 3dB down - you can't have everything at once.

Distortion looks distinctly second-ish, whereas the limiting mechanism is clipping in the balanced second long-tailed pair. This should be a symmetrical phenomenon and only produce odd-order distortion products.

The base terminals are internal to the circuit and so inaccessible, but not so the first LTP. Suspecting offsets in the long-tailed pairs, I added a 100k pot across the +15 and -15V supply rails with a 150K resistor from the wiper to pin 15.

Adjusting the pot, the distortion is reduced from 0.3% to 0.2%, nearly all third harmonic as expected. Reducing current into pin 2 further to give an output of 2V pk-pk produces a distortion at 1kHz of less than 0.08%. But at this low output level, the Q drive current needs readjusting at each frequency.

Idea waiting for a use

The SSM-2044 is undoubtedly a versatile and interesting IC. I am sure that one day I shall find it just the solution for some job or other, along with some of its stable-mates

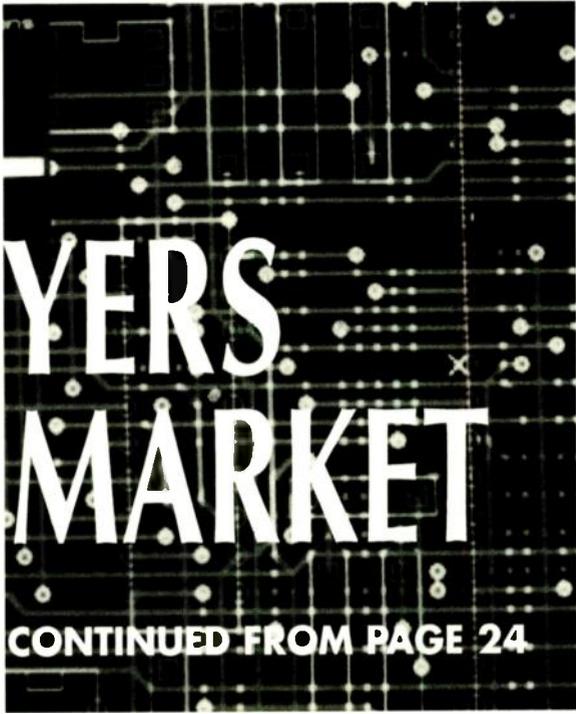
WITH C IMPORTANT ANNOUNCEMENT.

Many readers have been disappointed that **Howard Hutchings'** practical guide to real-time programming and use of the **C programming language for electronics engineers** sold out so quickly.

As a result of this popular demand, we are reprinting **"Interfacing with C"** and new copies will be available from the beginning of December.

To order, send a cheque for £14.95 to Lindsey Gardner, Room L333, Quadrant House, The Quadrant, Sutton, Surrey SM5 2AS. Make cheques payable to Reed Business Publishing Group or, for immediate response, you can telephone your order quoting your credit card number on 081 661 3614 (mornings only please).

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BUYERS MARKET

CONTINUED FROM PAGE 24

Graftool

Graftool is a 3D graphics package with features including: linear and nonlinear curve fitting; unlimited zoom and rotation; multiple axes in linear, log or probability scales; more than 268 million data points; scientific spreadsheet that can directly read Lotus and ascii files; unrestricted placement of graphs and text; and compatibility with Microsoft Word and WordPerfect.

Suppliers: Adept Scientific.

HiWire II

HiWire II is schematic capture and PCB layout software package for use on IBM PCs and compatibles. It is based on a menu-driven interface which simplifies common operations such as extracting a net list, creating a bill of materials, producing check plots, and plotting final artwork.

Suppliers: Riva; Wintek.

Isis

The Isis range of schematic capture software has three products - Supersketch, Designer and Designer+. All have a graphical user interface and an intelligent diagram editor. They run on PC compatible hardware and can interface to other cad packages.

Suppliers: Labcenter Electronics.

LCA1

LCA1 is a logic simulator program for running on PCs and compatible computers. A less powerful version of the package is called Bitspice.

Suppliers: Those Engineers.

LM-2

LM-2 is a logic synthesis program that can create Boolean algebraic expressions from a truth table. It will also handle state logic so flip-flop devices can be incorporated. The package is particularly applicable to dealing with programmable logic devices. Results can be ported to LCA1 so that the timing can be checked before building the circuit.

Suppliers: Those Engineers.

Mathcad

Mathcad is a mathematics package. The user types equations and they are automatically for-

matted into mA notation. The screen can be used as a blank piece of paper to let the user lay out the equations along with pictures, plots and text. Mathcad is designed to run on PC, Macintosh and Unix systems.

Suppliers: Adept Scientific.

Maxi/PC

Maxi/PC is a PC-based PCB design tool with features such as schematic capture, component placement, automatic and interactive routing, and manufacturing outputs for complex PCB systems. It is compatible with Cadstar.

Suppliers: Option Circuits, Racal-Redac.

MaxRoute

MaxRoute is a PCB autorouting package that interfaces with most of the popular cad systems. It uses push and shove technology to emulate the way a manual designer works and also contains a complete suite of interactive design tools. Runs on a PC.

Suppliers: GDS PCB Design.

Micrologic 2

Micrologic 2 is for simulating logic gates and includes a library of components for Boolean functions etc.

Suppliers: Data Technology.

OrCad

There are more than 50,000 users of OrCad electronic design automation tools. In release IV the schematic parts library has been increased to more than 20,000 parts, the digital simulation process has been speeded up, the PCB layout package offers autoplacement and autorouting at no extra charge, and there is expanded memory support. It works on PCs or Spare workstations.

Suppliers: ARS Microsystems; OrCad.

Pads-2000

Pads-2000 was the first cad system designed to run exclusively on 386 and 486 based PCs, and the first to run 32bit code with virtual memory. It provides all the tools needed to design a PCB including automatic component placement, 100% rip up and retry autorouting of traces, on-line

DRC, and automatic engineering change verification.

Suppliers: Cad Services; Cad Software; Cavendish Automation.

Pads-PCB

Version 4.0 of Pads-PCB adds a complete new graphics and user interface to this popular PCB design package. Other extras include the use of pop-up menus, a user definable macro language, and support for high resolution VGA graphics cards. There are more than 500 Pads-PCB packages installed in Great Britain.

Suppliers: Cad Services; Cad Software; Cavendish Automation.

Pads-Logic

Version 2.0 of Pads-Logic shares the new graphics interface, plotter outputs and library capabilities of Pads-PCB 4.0. This schematic capture system was introduced in 1990 and more than 2000 systems are in use world wide.

Suppliers: Cad Services; Cad Software; Cavendish Automation.

P-Cad Master Designer

More than 18,000 PCB designers use P-Cad Master Designer. The suite of products include schematic capture, symbol library, digital and analogue simulation tools, placement tools, routers, and design rule checking.

Suppliers: Cadam, KGB Micros.

PCB II

PCB II is a PCB design package available either stand alone or as part of an Ares or Isis package. Features include GUI, topological route editor, 2D drawing capability, and package library.

Suppliers: Labcenter Electronics.

PCS

PCS stands for process control simulation. This package is a training tool to show how to tune three-term controllers used in the process industry. It runs on a PC.

Suppliers: Golten & Verwer.

PSpice

The PSpice family includes circuit analysis and circuit synthesis packages and can run analogue and digital packages concurrently under dos. It has virtual memory capacity, filter synthesis and an optimiser for arbitrary transfer functions.

Suppliers: ARS Microsystems; MicroSim; Riva; others

Pulsar

Pulsar is a digital logic circuit simulator program for testing designs rather than going through time consuming breadboarding. Simulation speed is more than 1000 gate state changes a second. It runs on 386 or 486 machines.

Suppliers: Number One Systems.

Quick Plot

Quick Plot is a memory resident program for producing a graphics screen dump from a 286 or 386 PC on to an HPGL or compatible pen plotter.

Suppliers: Number One Systems.

Satcam

Satcam is used for PCB design and runs on a PC. Facilities include schematic capture, PCB layout, design rule checking, and autorouting. It has a library of stored components with about 25,000 entries and can carry out functions like photoplotting. It can interface with AutoCad. Satchem schematic capture package is available separately.

Suppliers: Data Technology.

Schema

Schema is a schematic capture PCB package for use on IBM PC or compatible computers.
Suppliers: *Auto Matrix.*

Spiceage

Spiceage is a simulator for small analogue circuits. See ECA2 for more details.
Suppliers: *Those Engineers.*

Supermax

Supermax is an extension of IPL software and offers schematic circuit layout, circuit simulation, schematic capture, automatic placement, and thermal analysis. It can run under Unix or on 386 and 486 PCs.
Suppliers: *Cadniques.*

Susie

Susie is the world's best selling PC-based logic simulation program that simplifies digital design by getting rid of the breadboarding stage. It uses advanced logic simulation software to create a working model of hardware design.
Suppliers: *Aldec; Computer Solutions; Option Circuits.*

Tango PLD

The Tango PLD design language is a development tool for programmable logic devices. It allows data entry either as schematics or using a version of C. A schematic diagram input approach allows a logic diagram or net list to be used to describe

the components required.

Suppliers: *Accel Technologies; Computer Solutions.*

Traxstar

Traxstar is a grid based costed maze autorouter with full rip up and reroute capability. It works on 386 machines and incorporates a user definable cost structure that allows separate cost structures for the route, rip-up and smoothing packages.
Suppliers: *JAV Electronics; Protel Technology.*

Traxview

Traxview is an RS274 Gerber format file viewer and editor. It lets users view files by zooming and panning. There are full editing facilities including placing, deleting, moving and editing of flashes and strokes. It also has block commands and a panelisation program that lets users place multiple Gerber files on the same film. Runs on 386 PCs.
Suppliers: *JAV Electronics; Protel Technology.*

VHDL 2000

The VHDL 2000 simulator is a full featured VHDL 1076 design analysis environment that supports comprehensive debugging facilities. It uses a simulation kernel optimised around the VHDL paradigm and is written in C++ with an object orientated database.
Suppliers: *Racal-Redac.*

Visula HPE

The Visula HPE suite of tools analyses the impact

of physical layout on the integrity of the electronic design of systems on boards. It can directly control the physical layout process from design rules which govern factors such as path delays, reflection and crosstalk limits.
Suppliers: *Racal-Redac.*

V-System

V-System is a complete VHDL development environment including an IEEE1076 compliant compiler, simulator and debugger for either the Windows environment on a PC or on a Sun SparcStation.
Suppliers: *Instrumatic.*

Vutrax

The Vutrax schematic capture software is a stand alone hierarchical schematic drawing package with features for connection validation. Documentation can be produced including net lists, part lists, wiring schedules, engineering cross-reference tables, and check lists. It is for 286 and 386 PCs.
Suppliers: *Computamation Systems; Those Engineers.*

Z-Match II

Z-Match II is a software implementation of the Smith chart analysis tool for RF engineers. It keeps all the graphical advantages of the original chart but has features that eliminate repetitive calculations and make the chart more accessible to the occasional user.
Suppliers: *Number One Systems.*

DIRECTORY

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ALS Design, 38 Rue Fessart, 92100 Boulogne, France. +33 1 46 04 30 47.

ARS Microsystems, Herriard Business Centre, Alton Road, Herriard, Basingstoke RG25 2PN. 0256 381400.

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Golden & Verwer, 33 Mosely Road, Cheadle Hulme, Cheshire SK8 5HU. 061-485 5435.

Hawke Systems, Newlands Drive, Poyle, Slough, Berkshire SL3 4DX. 0753 686676.

Instrumatic, First Avenue, Globe Park, Marlowe, Buckinghamshire SL7 1YA. 0628 476741.

JAV Electronics, Unit 12a, Heaton Street, Denton, Manchester M34 3RG. 061-320 7210.

KGB Micros, Lords Court, St Leonards Road, Windsor SL4 3DE. 0753 696069.

Labcenter Electronics, 14 Mariner's Drive, Bradford BD9 4JT. 0274 542868.

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Protel Technology, GPO Box 204, Technopark, Dawsings Point, Hobart, Australia. +8102 73 0100.

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Those Engineers, 106A Fortune Green Road, West Hampstead, London NW6 1DS. 071-435 2771.

Tracks, Meadows, Coppid Beoch Lane, Wokingham, Berks RG11 5PJ. 0344 55046.

Tsjen, Cambridge Research Laboratories, Huntingdon Road, Cambridge CB3 0DJ. 0223 277777.

Wintek, 1801 South Street, Lafayette, Indiana 47904, USA. +1 317 448 1903.

TrimDAC – an electronic pot

Analog Devices's TrimDAC is a multi-channel D-to-A converter meant to eliminate mechanical potentiometers for circuit adjustment. Setting circuit parameters becomes a matter of software control and the benefits of hands-off control, accuracy and a high level of reliability not to mention the eight controls in one skinny-dip package, are offered. The main impetus for development of the device is cost reduction in manufacture, calibration and field adjustment.

An example is the factory adjustment of CRT displays, in which convergence and colour purity must be set. In a 1000-line display, up to eight pot settings have to be made – an expensive business in high-volume production, robot-controlled screwdrivers being the usual method of adjustment. This can take several minutes to complete, whereas the TrimDAC will do it in seconds.

First-generation TrimDACs, DAC-8800s, are CMOS devices intended for DC control and contain eight unbuffered voltage-output

D-to-A converters whose outputs are independently set. Figure 1 shows the layout; eight DAC registers receive their contents from a TTL-compatible, three-wire serial interface, a CLR input allowing zero-setting for system power-up. An 11-bit word into the serial shift register is decoded and used to determine which DAC register is to receive the eight data bits, all eight being loaded in about 14µs. External voltage references determine the voltage output range, but DAC-8800 is primarily meant for fixed-reference DC voltage control.

Figure 2 is the block diagram of a second-generation TrimDAC, the DAC-8840, which extends the capability to the control of alternating voltages in, for example, audio volume control, video displays, modems, oscilloscopes and many other applications.

This device contains eight four-quadrant multiplying D-to-A converters. Each has a 1MHz bandwidth for ±3V input levels; THD is 0.01% and slewing rate is 2.5V/µs and, since the output amplifiers are of the differencing type, gain can be anything from

full-scale positive to full-scale negative under the control of the input binary word.

A typical application of the 8840 is in the adjustment of video deflection waveforms, as shown in Fig. 3. The four-quadrant multipliers adjust the sawtooth waveforms, reference bias voltages and the parabolic waveforms, the three being summed to drive vertical and horizontal deflection coils.

There are two slight drawbacks to the use of TrimDACs in place of pots, both of which are reducible: one is the fact that a pot "remembers" its last setting, even without power, and the other is the presence of the "zipper" noise when an audio volume control is adjusted that results from the digital nature of the device. The first is avoidable by using system memory to reload set points at power-up and the second minimised by capacitive smoothing of the voltage-controlled amplifier controlled by the TrimDAC.

Analog Devices Ltd, Station Avenue, Walton-on-Thames, Surrey KT12 1PF. Telephone 0932 232222

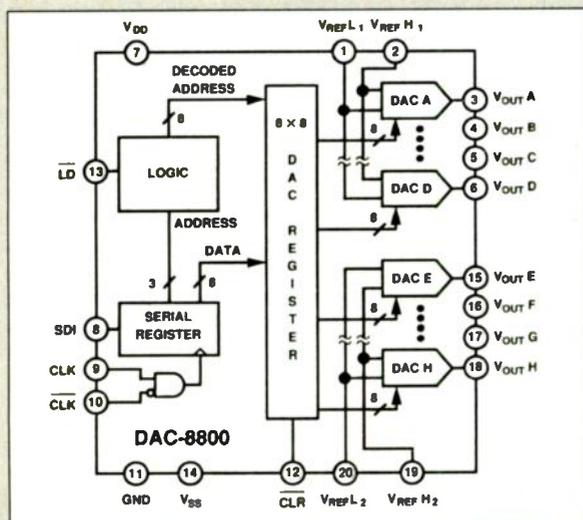


Fig. 1. Internal layout of Analog Devices's DAC-8800 TrimDAC for the replacement of mechanical potentiometers in the adjustment of direct voltages.

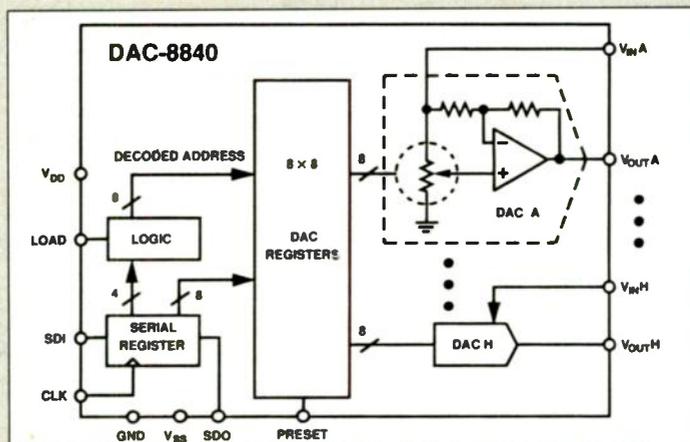


Fig. 2. DAC-8840 second-generation TrimDAC for AC control, which uses multiplying D-to-A converters for the combining of inputs.

Fig. 3. One application of the 8840 is the combining of deflection-correction waveforms for CRT displays.

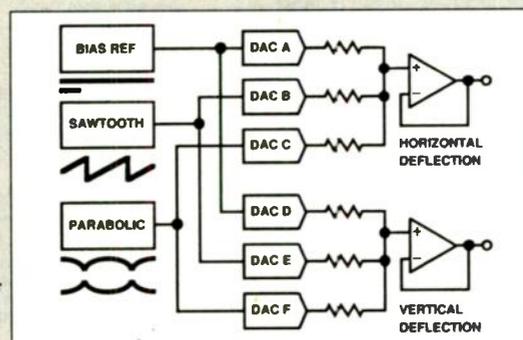
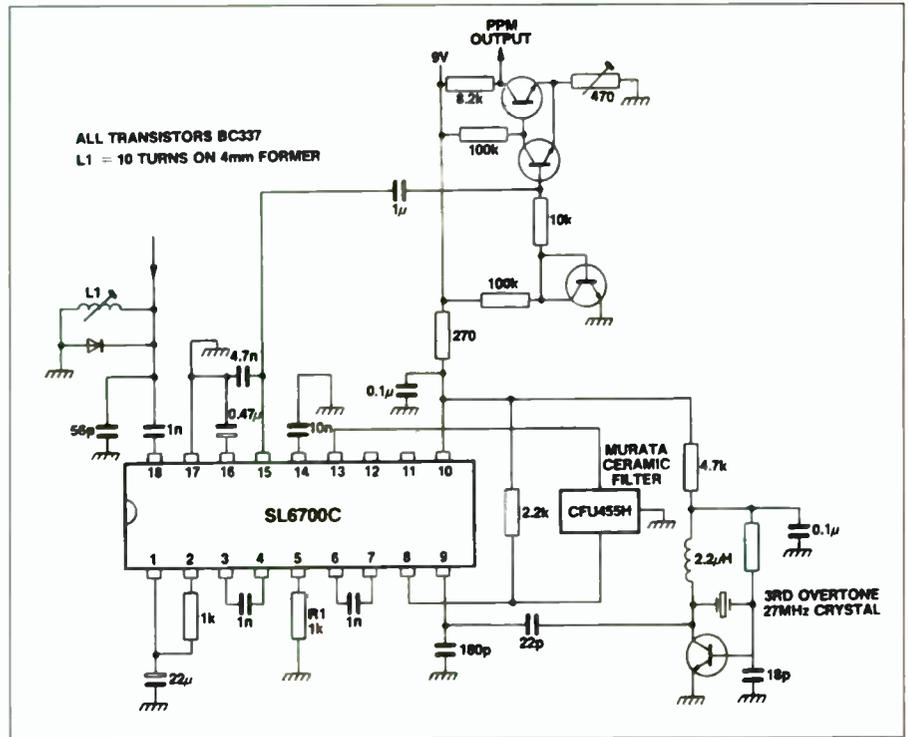


Fig. 4. 27MHz model-control receiver, which will operate on 4.5V with quite small circuit changes.

application – a model-control receiver for 27MHz working. A supply of 9V is a little high, particularly for aircraft, but the SL6700 is flexible enough not to need extensive modification for lower supply voltages. In this instance, only the oscillator will need changing to work at, say, 4.5V. To reduce component count, omit R₁ and the network on pin 18, which can be replaced by a Murata SFE 27MA4 ceramic filter. This receiver takes 5mA at 4.5V.

The application note, taken from the 1991 Professional Products IC Handbook, goes on to describe an AM/SSB/CW IF strip and, using an SL6700 in conjunction with an SL6270, an SSB generator.

GEC Plessey Semiconductors, Cheney Manor, Swindon, Wiltshire SN2 2QW. 0793 518000.



Protecting RF power transistors

Load mismatching can cause a high current in RF output transistors and increase power dissipation to the point of failure. Moreover, with temperature time constants in the region of 0.5 to 1ms, any attempt to counteract the effect does not have much time in which to operate.

Commonly, a reflectometer VSWR sensor between output and load produces a voltage dependent on output mismatch, which is used in earlier stages to decrease power or shut down completely.

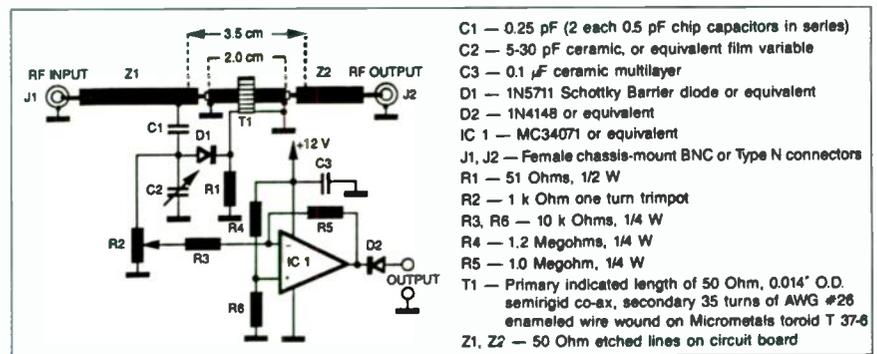
Motorola's application note AR510/D describes such a method. Figure 1 shows the principle, which is usable at VHF and UHF with lumped-constant design and up to the microwave region using stripline methods. In the former realisation, current in the amplifier output line is passed through a pickup coil, the two forming a tightly coupled transformer. The voltage from the pickup coil secondary is proportional to the output current and is compared with a voltage from the output line appearing at the junction of capacitive divider C₁C₂. When the load is matched, the two voltages are 180° out of phase. C₂ being adjusted until the potential divider voltage is zero.

Output from the MC34071 will operate as seen in Fig. 2, in which it turns off the bias voltage of a mosfet, either controlling the existing bias voltage or forming the bias source itself, as in the centre diagram. The only problem with this arrangement is that, while it is fine for a fast shutdown (2μs), linear operation is not possible, since a steady idle current is needed. For linear working, the layout in the right-hand

diagram is used, in which sensor output is used to control a low-level PIN-diode attenuator.

Motorola Ltd, European Literature Centre, 88 Tanners Drive, Blakelands, Milton Keynes MK14 5BP. Telephone 0908 614614.

Fig. 1. Protection circuit against load mismatching for RF power transistors. VSWR sensor goes between amplifier output and load, mismatch causing op-amp output to control or shut down RF output.



- C1 – 0.25 pF (2 each 0.5 pF chip capacitors in series)
- C2 – 5-30 pF ceramic, or equivalent film variable
- C3 – 0.1 μF ceramic multilayer
- D1 – 1N5711 Schottky Barrier diode or equivalent
- D2 – 1N4148 or equivalent
- IC 1 – MC34071 or equivalent
- J1, J2 – Female chassis-mount BNC or Type N connectors
- R1 – 51 Ohms, 1/2 W
- R2 – 1 k Ohm one turn trimpot
- R3, R6 – 10 k Ohms, 1/4 W
- R4 – 1.2 Megohms, 1/4 W
- R5 – 1.0 Megohm, 1/4 W
- T1 – Primary indicated length of 50 Ohm, 0.014" O.D. semirigid co-ax, secondary 35 turns of AWG #26 enameled wire wound on Micrometals toroid T 37-6
- Z1, Z2 – 50 Ohm etched lines on circuit board

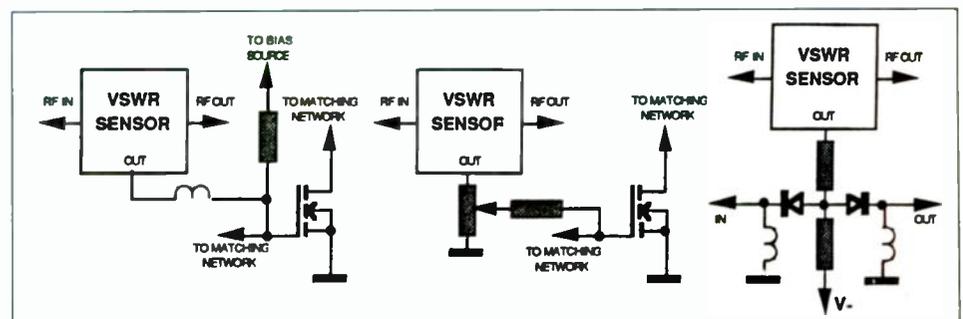
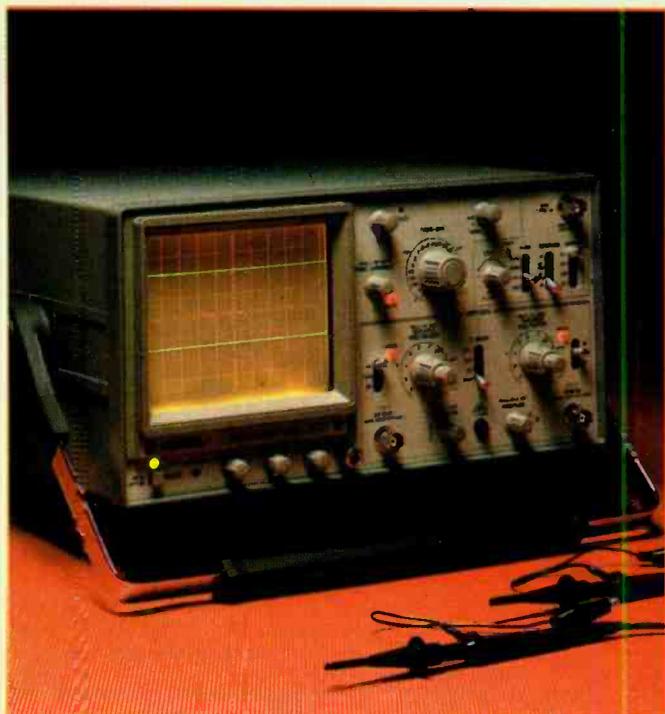


Fig. 2. Three possible methods of using VSWR sensor to control RF gain of amplifier. First two vary bias on mosfet and are useful for complete, fast shutdowns. Third method gives gain reduction for linear amplifier.

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SC110A miniature portable oscilloscope

■ **SC110A miniature portable oscilloscope**

The SC110A from Thurlby-Thandar is a full feature, single trace analogue oscilloscope packaged into the size of a benchtop multimeter. Fitted with a 32mm x 26mm screen miniature CRT, the bright, sharp image provides resolution and detail associated with much larger instruments. UK designed and built, the internal switch mode power supply draws just 195mA from four C sized batteries (not supplied). The instrument will operate from 4 to 10V DC.

The specification includes a Y bandwidth of DC to 10MHz, 10mV/div sensitivity and an adjustable brightline trigger with AC/DC/TV coupling from both internal and external sources. The X timebase is adjustable from 500ms/div to 100ns/div in 24 steps. The case measures 25 x 5 x 15cm and the instrument weighs about 1kg. SC110A £249+VAT (£292.58).

■ **1021 general purpose 20MHz oscilloscope**

The Model 1021 general purpose oscilloscope from Japanese instrument maker Leader Electronics more than meets its published specification and is of exceptional build quality. Features include 20MHz dual channel operation, 8cm x 10cm display area, 5mV/div Y1/Y2 sensitivity at 20MHz, DC to 500kHz X-amplifier response, variable trigger response, multiple sync conditioning and an overall accuracy better than 3%. 1021 £299+VAT (£351.33)



PL320K laboratory triple power supply

TS3022S laboratory dual power supply

PL320K laboratory triple power supply

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The analysis of electromagnetism presented last month does not take into account one of its most obvious characteristics: the enduring nature of permanent magnet fields.

It is hard to believe that permanent magnets are constantly emitting phaeons in the same kind of way as electrostatically charged objects. In contrast to the case of charged objects where the charge leaks away unless it is kept in a perfectly dry atmosphere and not heated or vibrated, permanent magnets can retain their magnetic fields for many years unless subjected to extreme stress, for example by being subjected to a larger opposing field from an electromagnet.

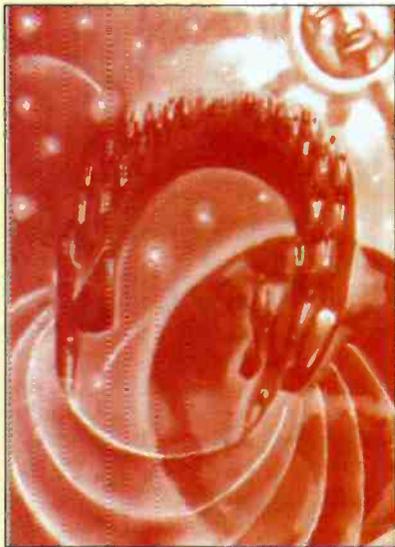
Another compelling feature of magnetic fields is their sense of being in some kind of continuous circulation. This can be illustrated by the importance of the vector curl function in magnetic fields, and in that the divergence vector of a magnetic field is always zero. Thus there is no source of a magnetic field in the sense of a charged object being a source for an electric field. Magnetic flux always forms a continuous loop.

We can expand the relativistic explanation of the origins of electromagnetism to account for these two properties (stability and circularity) of magnetic fields. However, it must be said that the analysis becomes extremely speculative at this point and leads to rather extraordinary conclusions.

From the discussion of the Lorentz transform given last month, we know that the linear separation of the atoms of the lattice of a wire appears to become smaller relative to the spacing of moving electrons when viewed from an electron in another conductor moving in the same direction as the electrons. We can define the direction that both sets of electrons are moving in as the positive z-axis. Think of the lattice of atoms of the metal as forming a series of x-y planes or plates across the wire. From the view of the electron in the second conductor, we can say that the trajectories of electrons in the first wire are compressed towards the x-y plane(s).

A fundamental part of the kinetic model

Scratching the surface of electromagnetism



is that an electron must rotate as it moves linearly through space. We can think of it in fact like a small gyroscope moving along the line of its spin axis. The relativistic compression of the electron trajectories towards the x-y plane can be thought of as a tilt in the electron trajectories towards this plane. We know that when we tilt a spinning gyro-

*Part two of
Scratching the
surface
postulates new*

*theories for photons and
protons*

scope about its spin axis a new force is generated acting at right angles to both the axis of spin and the applied force. (A good example of this force in action is seen when a cyclist leans sideways at a corner; the tilt of the wheels generates a sideways force which helps him turn the corner.)

The relativistic tilt of the electron trajectory within the ball produces a similar turning force on the electron. This force will be perpendicular to the tilt direction and the initial trajectory of the electron. This force will tend to curve the trajectory of the electron about the z-axis, and while the z-axis motion is maintained, the trajectory will continue to be curved. (Fig.10).

Furthermore, since this turning force will be always proportional to the forward component of electron velocity in the x-y plane, we can predict that the projection of the new trajectory on to the x-y plane will be the arc of a circle. Also, regardless of the initial direction of the component of electron motion in the x-y plane, the turning force

and hence direction of curvature will always be in the same direction about the z-axis for positive z-axis displacements.

We have already discussed the idea that when the electron is reflected from the inner surface of a surface the ricochet effect will twist the emitted phaeons and the reflected electron out of the plane formed by the line of incidence and the normal to the surface.

Now, just as the effects of relativistic changes will compress all initial electron trajectories towards the x-y plane, so the reflected trajectories will also be compressed into this plane. This compression tilts the trajectory of the electrons during the reflection process (tilts the ricochet) and we may conclude that an extra component of momentum needs to be lost (emitted) during the reflection process.

This extra momentum will be about the z-axis, and so the phaeon(s) emitted will have a component of rotation or spin about the z-axis. This raises a fundamental point: what is going to be the trajectory in space of a phaeon with angular momentum in two axes? Newton's Laws of motion tell us that a body must move in a straight line unless acted on by some external force. However the phaeon is like a gyroscope rotating in two axes at once, and therefore constantly tilting about the spin axis; and we know that a tilted gyroscope generates a reactive force at right angles to both the tilting force and the spin axis. We tentatively conclude that in this case Newton's Law does not hold, and that the trajectory of the phaeon as seen from the distant moving electron is, like the electron's, curved.

The curvature of the phaeon trajectories, however small, produces a fundamental change in the nature of the phaeon flux. We argue that the phaeons' trajectories are circular, and so the phaeons will eventually return to the wire from which they were emitted. Now, suppose we have a very large number of circular trajectories of different radii. To simplify matters we can just consider trajectories in the x-y plane as in Fig. 11a.

We can see that no matter how large the radius of curvature of the trajectories, if we

analyse the flux at any small region of space there will be as many phaeons returning towards the source as there are leaving it. Thus the net radial flux through an arbitrary region (eg that marked "alpha" in the figure) will be zero. The only non-zero component of momentum will be one tangential to circles around the emitting wire. This tangential momentum will have the same direction at all points around the wire. We can describe this effect as a circular "momentum flux" around the wire (Fig. 11b).

To sum up, we know from relativistic arguments that when electrons move through the lattice of a metallic conducting wire, there is a relativistic compression of the lattice as seen from electrons in another wire travelling in the same direction as the initial set. We have argued that because of the rotation of the electrons, this relativistic

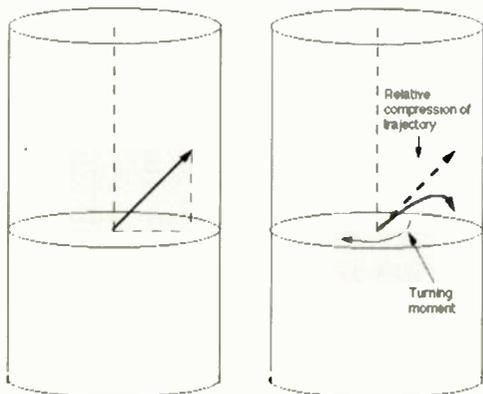


Fig. 10. Relativistic curvature of electron trajectories. Left: With no relativistic distortion the electrode trajectory is a straight line. The trajectory has a component in the z-axis and in the x-y plane. Right: The relativistic compression of the proton lattice as seen from another moving electron is equivalent to compression of the electron trajectory in the z axis. This compression generates a turning moment which curves the trajectory about the z axis.

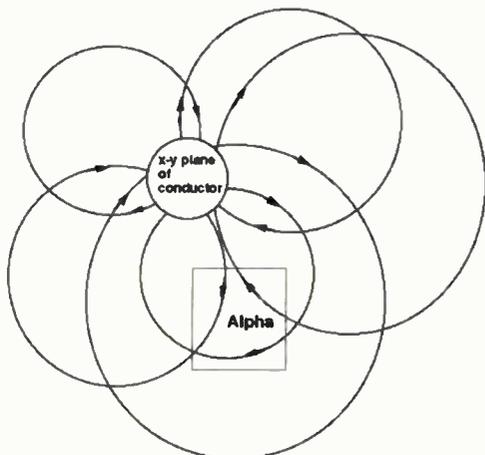


Fig. 11a. Relativistic curvature of phaeon trajectories. Because phaeons are emitted in all directions and thus return from all directions, the net radial flux through any arbitrary region of space such as that marked "Alpha" will be zero. The only non-zero component of momentum will be a component tangential to circles drawn around the conductor.

Fig. 11b. Net "Momentum Flux" around current-carrying conductor as seen from another moving electron.

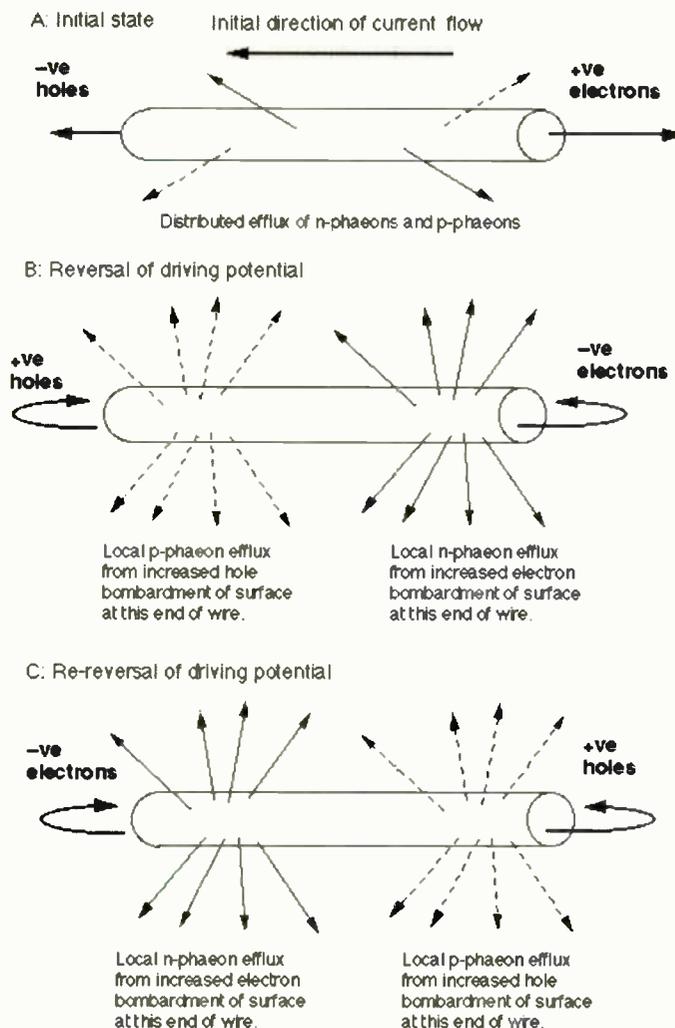


Fig. 12. Phaeon emission from an alternating current in a linear conductor.

compression acts to produce a curvature in their trajectories as seen from the electrons in the other wire, and when the electrons reflect at the surface of the wire, there is also a curvature induced into the trajectory of the emitted phaeons (assuming that such a particle exists - ed). This curvature in the phaeon trajectory changes the net phaeon "momentum flux" from a radial to a circular form.

The interaction of the changed flux and the curvature of the electron trajectories produces an imbalance in the surface forces on the sides of the conductors and a net force between the wires. The force is attractive if the electron flow is in the same direction, repulsive if the flow is in opposite directions.

We can now thus explain why permanent magnets do not "run down". The phaeons are constantly circulating, exchanging momentum with the electrons in the magnet; indeed, in one sense, we can think of the phaeon trajectories as a kind of extension of electron orbitals; an electron may lose momentum at one point by reflection but regain it at another point by absorption of

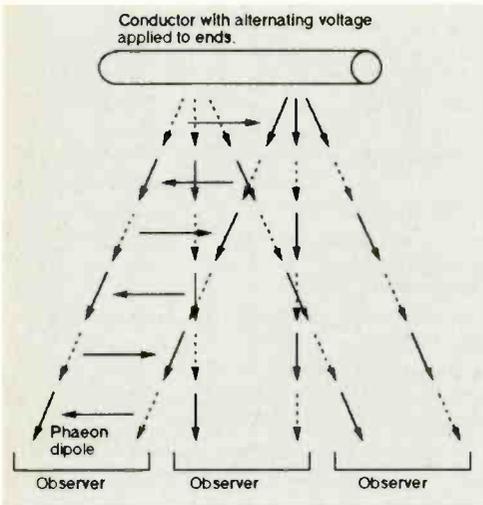


Fig. 13. Phaeon emissions from a conductor subject to an alternating voltage. Each observer sees a sequence of phaeon "dipoles" emitted from the conductor; with the polarity of the dipole reversing with each cycle of the applied voltage. (Dashed lines are p-phaeons, solid lines are n-phaeons.)

the same or a similar phaeon to that which it emitted.

Electromagnetic radiation

The reason electrons will move along a wire conductor will normally be the existence of an applied electric field. We can translate this into a "phaeon barrage". The electrons are "pushed" from one end by the impact of n-phaeons and "pulled" from the other end by the impact of p-phaeons. Under the influence of a steady potential, as we have seen in the previous section, electrons migrate one way through the conductor, and holes the other way, each colliding with the walls of the conductor as they move and emitting phaeons perpendicular to the current (Fig. 12A.)

Of course, in different conductors the proportion of the current carried by holes and electrons may vary enormously. In some semiconductors the current is carried almost exclusively by holes and in others almost exclusively by electrons.

Suppose that the direction of the steady applied field is then suddenly reversed (Fig. 12B). The electrons have finite inertia and so their direction of movement cannot be instantaneously reversed. Electrons will accumulate at the newly negative end of the wire - the electrons will effectively be transiently compressed in this region. Similarly holes will transiently accumulate at the newly positive end of the wire where the electrons are compressed will be greatly increased, and similarly the p-phaeon emission from the newly positive end will be likewise increased. Thus the phaeon emission will become polarised; one end of the wire will emit excess n-phaeons and the other will emit excess p-phaeons.

Eventually of course equilibrium will be

re-established and the normal electron and hole migration will be re-established in a reverse direction. If the potential is now reversed (Fig. 12c) the compression process occurs in reverse, with the region of the wire that first emitted n-phaeons now emitting p-phaeons, and vice-versa. We can see that the result of a relatively low frequency of an alternating field being applied to the wire is a sequence of simultaneous emissions of n and p phaeons from the two ends of the wire. If the applied frequency is high relative to the length of the wire, we might get harmonics formed, with several sites of emission of each type of phaeon from "nodes" where electrons or holes are momentarily compressed.

We assume that the phaeons travel at the speed of light. To an observer at some distance from the wire looking at it from the side, the emission of the bursts of n and p phaeons from the two ends of the wire will be detected simultaneously. We can think of a large number of n-p "phaeon dipoles" being emitted with each cycle of the applied field (Fig. 13).

The axes of these dipoles will be parallel to the wire and perpendicular to the axis of propagation of the phaeons. The dipoles will reverse direction each time the field applied to the wire reverses. What will happen when these phaeon dipoles meet electrons in recipient atoms or molecules? The linear momentum components of the n and p phaeons will cancel out, but the angular momentum com-

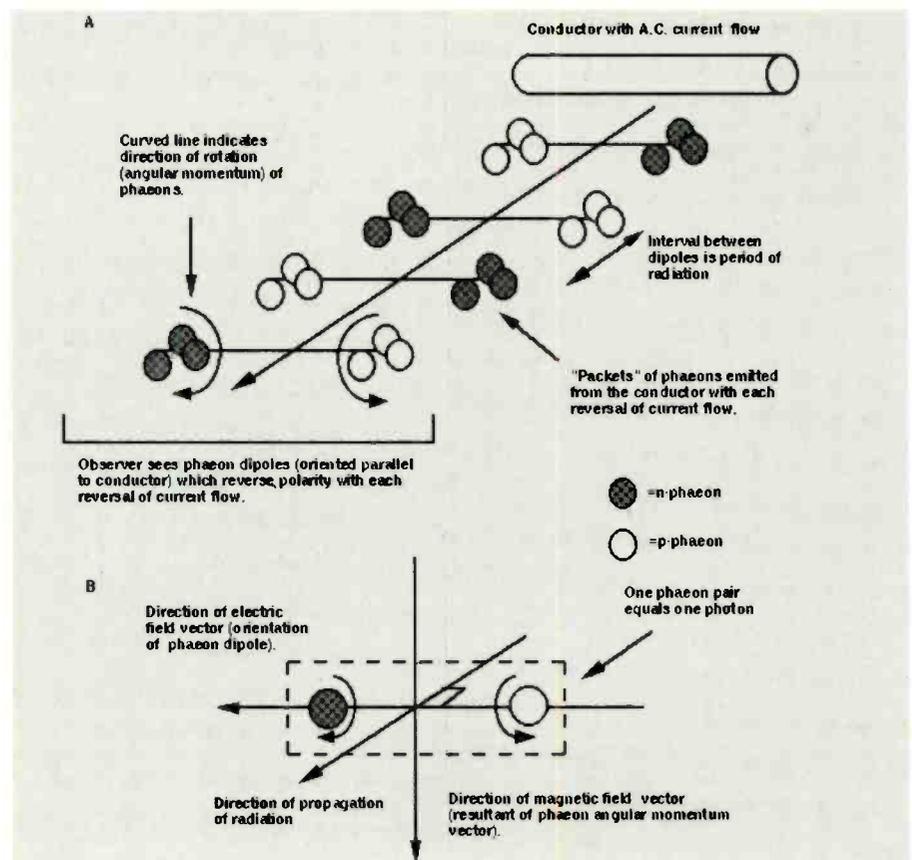
ponents could act to give recipient electrons some kind of increase in vibrational or rotational energy.

The ability of an electron in an atomic or molecular orbital to absorb the phaeons might well depend on the frequency of reversal of the dipoles; there might need to be resonance between the vibrational frequency of the electron orbital and the dipole oscillation frequency. The dipoles can be considered as the origin of an electric field oriented perpendicular to the direction of propagation of the phaeons. This field will reverse with each reversal of the dipole. Note that the rotation of the n and p phaeons is complementary and so there will be a net angular momentum associated with the phaeon dipole (Fig. 14).

The direction of this angular momentum vector will be perpendicular to the electric field vector and to the direction of propagation; like the electric field vector, it will reverse direction with each reversal of the dipole. This resultant vector we can tentatively identify with a magnetic field vector as in Fig 14B.

Both electric and magnetic vectors will of course reverse with each reversal of the dipole. We can now see that the phaeon pairs have the characteristics of the photons that carry electromagnetic radiation. Furthermore we have an explanation for the fact that a particle, the photon, has a frequency associated with it. We argue that photons are in fact phaeon dipoles, oriented perpendicular to the direction of propagation of the electromagnetic energy, which reverse in orientation with each radiation cycle

Fig. 14. Electric and magnetic fields associated with phaeon dipoles.



High energy photons are phaeon pairs which reverse at high frequencies, low frequency photons are phaeon pairs which reverse at low frequencies. When electromagnetic radiation is coherent, simultaneous emission of spatially separated n and p phaeons occurs. When spatially random simultaneous emission occurs, as from the conductor carrying a steady current, the phaeons can be detected in the form of heat energy.

In summary, we have generated a model of the photon which suggests that the photon is made up of two phaeons organised as a "phaeon dipole" which is perpendicular to the direction of propagation. The frequency of the photon is the frequency at which the dipole reverses its orientation.

The role of protons

According to the present model, all electrical and magnetic forces are due to the interactions of electrons and holes. Holes are virtual electrons, that is vacant orbitals around atoms that electrons could occupy but don't. The movement of holes can be thought of as a time-reversed movement of electrons. Thus ultimately all electromagnetic interactions are due to electrons, and the phaeons they emit when changing momentum.

The role of the proton can be seen as somehow deforming space so as to provide a set of "orbital spaces" at different energy levels around it. In one sense, a proton

defines and creates a hole; but does not define the energy of the hole. According to this model a proton is not itself charged in the sense that it acts at a distance on other charged objects. However, if a proton does not have charge, we need to explain the observation that a free proton is acted on by electric and magnetic fields. This is because in a solid object, the protons are fixed in the lattice and the holes are formed by the loss of local electrons. However, if a proton is free to move in an electric or magnetic field it acts like a mobile hole in a lattice, with one important difference.

The "inertia" of a hole in a lattice is the same magnitude as the inertia of an electron, as migration of a hole is a time-reversal migration of an electron. The inertia of the hole around a free proton is in contrast much higher as it will be the inertia of the proton itself. Thus we can predict that a free proton will move in a complementary way to a free electron in a magnetic or electric field, but with different velocity because of its different inertia.

Conclusions

There is not room in this article to discuss all aspects of a "kinetic theory" of electromagnetism. If there are aspects of electromagnetism that the model is completely incompatible with, the model will have to be discarded. Even if it is wrong, the model leaves attractive images behind: the idea of a

photon as an alternating "phaeon dipole" neatly explains how photons, which have neither charge nor magnetic dipole, do in fact combine both, but in a form which alternates at the frequency of the radiation. Conduction via holes is usually left in the hands of semiconductor engineers: the current model emphasises the essential symmetry between holes and electrons in the origins of charge and magnetism.

The puzzle of the identical magnitude of charge on protons and electrons is dealt with simply; positive charge is an expression of a lack of electrons, not some special property separate from the electron. The explanation of electrostatic forces emphasises the importance of surface forces and charge. Relativistic arguments are used to explain the link between charge and magnetism, but in an unusual way that also explains the importance of the curl of magnetic fields.

Perhaps the most radical aspect of the current model is the postulated role of the proton. If it does not indeed act at a distance as a source of positive charge but only acts locally to define a hole, much of our current analysis of intra-atomic forces may need revision.

My thanks go to T.G. Barnett who constantly urged me into print.

Dr Julian Millar is a medical physiologist at Queen Mary and Westfield College, University of London.

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LETTERS

Cause of illness

The article "Power lines, cancer and cyclotron resonance" by H Aspden (*EW + WW* September 1991) suggests that "a possible link between cancer and electromagnetic radiation from power lines... can be traced, experimentally, to a resonance effect known in physics as cyclotron resonance." The author goes on to suggest that the frequency of power generation and transmission should be changed from 50Hz to 100Hz to eliminate the supposed hazard.

We wish to state that there are no grounds whatsoever for believing that cyclotron resonance induced by the earth's magnetic field and a 50Hz electromagnetic field can exist in living organisms, or indeed in any electrolyte at normal densities.

It is not sufficient just to note, as Aspden has done, that the cyclotron frequency of the OH^+ ion, or of other ions present in the body, is close to 50Hz in the geomagnetic field (about $50\mu\text{T}$).

For a significant transfer of energy to occur even when the frequencies are exactly matched, the circular orbits of the ions must not be disrupted by collisions with other molecules or ions, so that they can be accelerated to large velocities. The average time between one collision and the next in an aqueous solution is about 10^{-11} seconds (this follows from simple estimates of the molecular density and thermal velocity).

Hence one orbit must be completed in rather less than this time to observe the resonance. In other words, the frequency must be above 100GHz. The frequency of power-line fields is too small by a factor of over a thousand million!

Since the proposed cyclotron resonance effect requires only the presence of ions in the body, any remaining doubts about its absence at 50Hz should be dispelled by looking at existing measurements of electromagnetic absorption in aqueous electrolytes at low frequencies.

However, measurements have also been carried out on bone and tissue, and they too show no sign of any resonant increase in absorption near 50Hz¹. The AC conductivity, which can be extracted from the absorption data by an application of Maxwell's

equations, typically shows no frequency dependence below 100kHz, above which motion of polar molecules causes dispersion.

Incidentally, there is also no justification for a frequency-pulling effect even if cyclotron resonance were operative, since the ionic concentrations are low and the AC magnetic field is weak; magnetic fields generated by the resonating ions are negligible.

We do not wish to imply that, because cyclotron resonance absorption is not a player, that there are no adverse effects resulting from long-term exposure to low-frequency electromagnetic radiation, whether at 50 or 100Hz. The recent CRC handbook on the biological effects of EM fields¹ documents many such effects on particular tissues and cells as well as on whole animals.

A useful summary of possible mechanisms has been given by Straub². An informed appreciation of current scientific knowledge in this area is an essential ingredient in the environmental debate concerning power lines, and this debate is ill-served by the article published in your magazine.

TC Choy, DR Hutton and DA Smith
Monash University
Clayton
Australia

1. Polk C and Postow E, "Handbook of biological effects of electromagnetic fields", CRC Press (1986)

2. Environmental Health Criteria v 16, "Radiofrequency and microwaves", World Health Organisation (1981)

Damming argument

A cyclotron uses a pumping system to produce a high vacuum in the space in which the ions are accelerated. This is because if an ion spiralling in a magnetic field is to pick up a significant amount of energy from an oscillating electric field it must be able to traverse several turns of its spiral path at resonance (usually one turn per cycle of the oscillating field) without being significantly deflected by collisions with other ions, atoms, or molecules. However Harold

BT parity line

Following the recent article and correspondence on the BT Phonebase service and its use of V23 data-rate, I should like to point out another problem that has so far been overlooked.

It should indeed be convenient for Phonebase to use the same V23 data-rate as provided by the mini-terminals universally used by European videotext services (Prestel, Télétel, Btx). But there is also the vital question of number of bits per word and parity bit protocol.

Prestel and Télétel use seven-bit/even parity, as did the original experimental Phonebase service.

That meant I could use Phonebase via a simple cheap interactive terminal connected to the phone which I also used to call Prestel and Télétel services.

But when Phonebase was relaunched, one of the giant intellects behind it decided that it would be a good idea to move further towards the ASCII VT-terminal standard by changing to eight-bit, no parity – pity they didn't think to tell the writer of the Phonebase manuals – and bang goes my useful little terminal, which can't be changed from the seven-bit/even standard of V23 videotext.

In fact very few terminals (as opposed to PCs) on the market can operate V23 in eight-bit/odd mode; almost all offer V23 seven-bit/even and, sometimes, V21 eight-bit/odd (300 baud).

So here we have an excellent up-to-date computerised database, wanted by almost everyone, owned by the largest and wealthiest communications technology company in the country, but coupled to an unbelievably amateurish access system.

No one could describe it as a large or complicated task to set up reliable, multi-speed access to such a database. There are hundreds of part-time enthusiasts running free bulletin boards across the globe that achieve infinitely superior performance, flexibility and complexity of interface.

I would be most interested to see if those directly responsible for the service could be persuaded to comment on this truly pathetic situation.

Alex Gray
BBC
Milton Keynes

Aspden's hydroxyl and hydronium ions ("Power lines, cancer and cyclotron resonance", *EW + WW*, September, and November and December letters) are immersed in tissue or body fluids, so that they undergo many thousands of such collisions during each mains frequency cycle, and no cyclotron resonance can develop.

Shareholders in National Power and PowerGen may therefore breathe freely once again.

In November letters DT Moore extolled the green virtues of hydroelectric power, but this brings its own hazards. It is known that filling the deep reservoirs behind some high dams in mountainous country markedly increases the frequency of earth tremors, and in one case has triggered a landslide. The resulting water surge breached the dam. In seismically active regions dam structures – because of the large hydrostatic stresses

imposed on them – are very vulnerable, and so are the people living downstream.

CF Coleman
Oxfordshire

Absorbing facts about ions

When Harold Aspden suggests cyclotron resonance as a means by which electromagnetic fields might produce biological effects (Power lines, cancer and cyclotron resonance, *EW + WW*, September, pp. 774-775); he overlooks a very important flaw in his argument.

During cyclotron resonance the ion's orbit is in phase with the electric field, such that it is only accelerated and never decelerated, over many orbits. So if the absorption of energy is to be any different from that of the simpler case of an oscillating ion in an AC

electric field, it must complete at least one orbit before it is significantly scattered.

A sodium ion, with average thermal kinetic energy ($3kT/2$), will have a speed of 500m/s, and if it is to make 50 orbits/s then the circumference of the orbit will be 10m. In reality an ion will be scattered within nanometres. An alternative way of looking at this, is that the resonance has a Q of, of the order of, a trillionth.

Harold Aspen might take note of the corollary that when there is no scattering in a simple cyclotron; there is still a limit to the energy; which is predicted by, and only by, relativity.

Robert Woolley
Imperial College of Science and Technology
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Active response

In his active filters article (*EW + WW*, October, pp. 812-818) John Linsley Hood correctly states that circuit details about active filter systems are not easily found, but then proceeds to introduce a curious hotch-potch of active and passive filter designs with, I feel, too little information to be useful, and at the same time containing a number of errors and misleading statements.

The circuit in Fig. 3 will not produce a flat or near-flat response with 1kHz cutoff; the LCR section as shown has a Q of 31.6 giving a 30dB response peak at 199Hz!

The terms Chebyshev, Butterworth and Bessel do not refer "broadly to filter types" as Mr Linsley Hood states. On the contrary, they precisely describe standard filter responses. The Bessel response gives maximally flat group delay (linear change of phase with frequency) but slow amplitude roll-off; the Butterworth response gives a maximally flat passband response, but with a peak in the group delay, and faster amplitude roll-off; the Chebyshev response gives still faster amplitude roll-off at the expense of ripples in the passband, and ripples and large peak in the group delay.

The pole positions for the low-pass versions of these, and other standard responses are quite often tabulated in filter design textbooks, typically for up to ten poles, though nowadays they are easy to calculate

on a PC, or even a pocket calculator.

Turning now to the filter circuits, the article shows a tuneable notch filter requiring a pair of ganged capacitors for tuning. This seems a perverse choice given that there are at least two simple notch filter designs using single resistor frequency control, which have appeared in *EW + WW*.

Figure 13 is described as an "active integrator with overall loop negative feedback that gives a flat Butterworth-style response" This circuit is usually known as the single-amplifier multi-feedback filter, and the two-pole low-pass version shown in Figure 13 can give any two-pole low-pass response, including Chebyshev, Butterworth, Bessel etc. This emphasises the point that these are response shapes, not filter circuit types.

Next take Fig. 14, the bridged-T; this is correctly described as a third-order type (because it has three reactive elements) but then the article goes on to claim that the third CR circuit gives a further 6dB per octave roll-off. This is only partly true: the extra pole provided by the third CR circuit is actually needed to cancel the parasitic zero that the bridged-T introduces. The extra pole is typically made to coincide with and cancel the zero, so that an accurate two-pole response results. The pole can be moved down to a lower frequency if the Q is set >1 so that at low frequencies, a three-pole response is obtained. However, above the cut-off frequency, the zero still affects the response, and it becomes two-pole again.

This same problem afflicts the bootstrap circuit (Fig. 16) for the same reason; the circuit values shown for the low-pass circuit give a 1.5dB passband ripple three-pole Chebyshev response up to and beyond the -3dB cut-off frequency, but the parasitic zero has cut this to a two-pole 12dB per octave response by about 2.5 to 3 times the cut-off frequency. A true three-pole response would continue to attenuate at 18dB per octave above the cut-off frequency.

The Sallen and Key layout is described by Linsley Hood as "able to give high-pass and low-pass Butterworth filters". Again, this circuit gives a two-pole response, and can therefore provide any two-pole response characteristic. Besides

Sporadic - E or spirit world?

I have recently come across a group of people who claim to have received images from beyond the grave on television sets. The phenomenon, known as TVEP (television electronic voice phenomenon) is promoted by a group originating in Luxembourg, (CETL, BP 02/Hesperange, Luxembourg) who claim to have a "hot line" to a spirit guide known as "Technician".

They appear to be surprised that many of the images seen are of famous German people, including National Socialists. One viewer is known to have been shocked that such evil people have gone to heaven. Another image received was of Hannah Buschbeck a famous ESP (extra sensory perception) personality who died aged 84. However her image was when she was 30 "because she did not wish to project herself as an 84 year old". It is claimed that the image has been identified with photographs of her taken when she was 30.

The idea of intermittent long distance TV reception of films and documentaries does not seem to have occurred to the group, and they doggedly persist in sending out videos, newsletters and so on. One individual claims that there is a world-wide cover up, sponsored by governments and the churches who apparently don't want the populace to receive the "proof" that there is life after death and that contact can be made with the dead. The alleged motivation for this cover up is not known to me.

There is a story going round that in 1955 or 1956 a Mr H Reeves who lived on the south coast on a hill, appeared on British television, possibly on the evening news magazine *Highlight*. He related how he received a spirit message on his television from Technician and a group called Timestream. He was later confused with Mr Alec Reeves, the inventor of PCM who was also interested in ESP.

If any reader has a recollection of this broadcast about Mr H Reeves' activities, I would be grateful to have details, because as someone who knew Alec Reeves I am asked about this.

I would also be interested to hear from anyone who knows of a television play or film broadcast in the mid 1950s - snatches of which may have been received by Mr H Reeves by sporadic E or meteor scatter - that contained a character called Technician and a group called Timestream. It could have been an early regional ITV play.

Best of all, of course, is the possibility that Mr H Reeves is still alive and reads *EW + WW* and is willing to contact the group.

John de Rivaz
Porthtowan
Cornwall

low-pass and high-pass, it can also give a bandpass response as can, incidentally the multi-feedback and bridged-T layouts (but not the bootstrap).

The all-pass filter construction shown in Fig. 23 (labelled "The" all-pass filter) is not very useful since it has a fixed Q or zero (single-pole response). The function of the adjustable resistor is not clear, since the all-pass response is only available at the junction of the C and the end of the variable resistor. The all-pass response (but with adjustable Q) is the means by which a filter with the required amplitude response, but not phase response can be made to have the required phase

response as well.

Lastly, Fig. 22 shows how a flat bandpass response can be obtained by cascaded HP and LP sections. While this will work, it will give poorer slopes near the pass-band edges for the same number of stages as the more conventional approach of using cascaded bandpass sections.
Brian J Pollard
Watford
Herts

Less loss

Mr Linsley Hood's article on active filters (*EW + WW*, October, pp. 812-818) was most interesting. Your readers should, however, be aware

that the low-pass and high-pass second order responses given by the bridged-T feedback configuration and by its variant, the "bootstrap" circuit, have an ultimate attenuation band fall-off rate which is theoretically 20dB/decade less than that which would be obtained by designing the filters to make use of Sallen and Key (or equivalent) second order sections. In multi-pole filters, the loss in ultimate fall-off rate will approach 20dB/decade for each such section.

A Kraicer
Edgware
Middlesex

Dab hand

The entertainment industry is to be congratulated for pioneering FM, TV and now dab. FM is used for much more than broadcasting today; TV is used in medicine, teaching, astronomy, etc; and now dab will revolutionise mobile radio communications, fixed multiplex links, telecommunications in general

and our lives in particular.

Your dab review article (All systems go for dab?, *EW + WW*, October, pp. 880-882) raises the following thoughts. If one block of 1.5MHz of radio spectrum can carry some 12 (six stereo) channels of 15kHz audio information this is the equivalent of 180kHz of analogue bandwidth with a dynamic range of more than 100db. That is roughly equivalent to 60 mobile radio channels using a 25kHz RF bandwidth.

Restricting the frequency response of each channel to the audio range of 300-3000Hz and the dynamic range to 60db the RF bandwidth requirement can surely be reduced to well below the 25kHz (FM) often in use today for mobiles. Using trunking techniques, Eureka style dab with its mutual interference cutting characteristics and low RF power requirements will allow implementation of mobile radio schemes with a lavishness that lack of RF spectrum has denied all these years.

After a decade of resistance on the

part of the BBC to non-compatible FM stereo radio broadcasting it is good to see that at last the old lady has seen the light. A pity indeed that the price is that BBC researchers are so little involved, since dab is really what their business is all about.

Peter Hirschmann
Haifa Israel

Fluke details

The Fluke 80 series multimeters feature an ultrasonic data output facility for which, for some obscure reason, Philips is resolutely unwilling to provide details.

I would like to ask whether any *EW + WW* readers have successfully built an interface to the multimeter using this interface and have been able to decipher the data protocol. I would be very grateful for the advice and can be contacted on 0272 741918.

Paul Johnson
Clifton
Bristol

Criticism reviewed

It is apparent that the reviewer of my book *CTG Capacitance Theory of Gravity*, failed to grasp the concept of a voltage tcegradient field in dimensions of volts per daraf through capacitance-dominated space, which is much like a volts per ohm field through resistance-dominated space. These fields were explained in pages 23-36 and in Appendix D. Volts/daraf equates in MKS(R) dimensions to coulombs, just as volts/ohm equates in MKS(R) dimensions to amperes. The dimensions remain balanced and true when converted and equated with MKS(NR), CGS, ESU, and EMU. The force, Q-times-the-volts-per-daraf, which is not in "newtons" (as explained on page 36 but misinterpreted by the reviewer), was therefore designated with new amplitude-equivalent-for-MKS called "gravits". Then 1 gravit = A newtons, where A is equal to one newton/gravit, or 1 daraf/m. When the F_g gravity force and A dimensions are both converted to other dimensional systems, no errors occur in either amplitude or dimensional balance.

In the CTG book, instead of A, amplitude-equivalence vertical brackets were used throughout the book to designate "gravit" force equivalence to "newton" force, as

MKS units were used exclusively.

As far as demonstrating that electric field coulomb law forces disappear in the CTG theory, this was explained on pages 27 through 29. Electric fields from myriads of closely spaced plus and minus poles of dipoles with random orientation cancel at any point in space, hence no coulomb law forces.

I do hope that readers of *EW + WW* are not sufficiently persuaded by the negative review to make no judgement for themselves and will take a look at this new concept. Other reviews have been more comprehensive and more positive.

Morton F Spears
Spears Associates Inc
Norwood
Massachusetts
USA

Thanks... for the memories

A while ago I wrote asking for your help in looking up old issues of *Wireless World* to find data on the RAF receiver R1155. The response has been remarkable. Complete strangers have put themselves to all sorts of trouble on my behalf out of sheer good nature and, one can infer, some nostalgia. Your help has been invaluable. Thank you indeed.

But much wants more - my R1155 is my second priority request - my first is to obtain another ex-government receiver for long waves only, 15-200KC. Two receivers were made - one, code B28 (Marconi R100) was a general coverage one; the other, similar in appearance, code B29, covered the VLF spectrum. I have tried in vain in every way open to me to find one. True they are likely to be scarce, but they were on the disposals market in 1960 and there may be one tucked away somewhere. Can anyone help?

Douglas Barry
Ward of Turin
Rescobie
By Forfar
Angus

Vintage stuff

Can you help me to find a home for some 1940s equipment which I should like to donate to a good cause. The collection includes a TF144G, TF517F, Type 13 scope, RAIB communications receiver and an ARR-3 sonobuoy receiver.

The items were on offer to the

ABC of amplifiers

The amplifier circuit suggested by WO Richards in Circuit Ideas, *EW + WW*, October 91 seems to be a neat up-date of the design approach described twenty years ago by Peter Blomley (New Approach to Class-B Amplifier Design, *WW*, Feb-Mar 1971). In that design, cross-over distortion was avoided completely by transferring the switching function from output to an earlier stage which divided the signal into "top" and "bottom" unidirectional halves. With the output stage biased just into conduction, the signal halves drove their respective output stage halves like class-B but without entering the cut-off area, and united in the load in the usual way. An amplifier using the system had a performance that may not be bettered today.

Why then, did it not sweep class-B off the market? One reason might be the patent application mentioned with the article. Blomley himself considered his design wasted on the transducers of the time. Many music-lovers are quite happy with their class-B equipment. Nevertheless, ears do twitch at cross-over distortion and the excellence of CD and (some) broadcasts bring a desire for amplifiers worthy of them. So anyone who tries the Blomley system simply for own interest may become quite pleased. (Yes, there are still plenty of audio hams - ask the firms who supply parts and kits). It would be helpful if Mr Richards would supply some performance details. Capacitive coupling may upset some purists. I am more concerned by the different total values in the two halves of the amplifier.

Finally, is it class-A or B? It operates in the class-A area but does not require a standing current large enough to meet the heaviest likely demand. Like class-B it draws current proportional to drive but operates clear of the cross-over area. Class-AB is what many circuits are already. What about class-BA?

W Groome
Wolverley
Worcestershire

Communications & Electronics Museum Trust at Bristol, but this now seems to have disappeared through a hole in the ground. I have tried to find other museums or collections of vintage electronic gear to which I could give these bits, but so far no one has been able to help. Of course I have heard of the Vintage Wireless Company, but that is a commercial operation, generally more concerned with the cosmetic details than with the gear per se.

Michael Hawkins
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RDS voids

With reference to Philip Darrington's "RDS on the road" (*EW + WW*, November, pp. 973-974), his statement that RDS data "is now carried on all FM Transmitters in the UK" is blatantly not true. Even if the statement referred to the BBC only, it would still be incorrect.

The BBC has many transmitters, mostly in Scotland which do not carry RDS data; eg some sites bordering the A9 from Perth to Inverness, sites in the Western Isle and also sites on the north west coast of Scotland carrying mono transmissions only. The BBC did admit to this, when pressed, at the Motorfair in London recently.

National Transcommunication Ltd (NTL) formerly the IBA have many local independent stations not carrying RDS data; eg Beacon Radio (Wolverhampton), Fox FM (Oxford) and Moray Firth Radio (Inverness) to name a few.

In addition, NTL have stations with dual sites and frequencies which do not carry AF listing, and so RDS radios will not retune as signal strengths vary; eg Radio 210 FM (Reading) has 102.9MHz from Hannington and 97.0MHz from Reading with neither carrying AF listing. As an extensive RDS user (both in UK and Europe) I find the UK well below average on operational techniques employed. My main frustration is the manual operation of the TA override command from studios. European Stations have automatic switching when the traffic announcement jingle tape is inserted and so drivers hear all the Traffic Announcement. UK stations employ manual switching and unless studio

operators switch the TA on during the jingle tape, the start of the announcement will be lost.

I understand take up of RDS in the UK is very slow, but until the system is fully operational and studio operators are correctly trained, take up will continue to be well below our European partners.

Terry Parrott.
Hampshire

Tuner kit

The article "RDS on the road" (*EW + WW*, November 1991) prompts me to wonder whether any manufacturer produces a unit, or kit, which can be connected to a conventional FM tuner to give an RDS display. Can any reader or manufacturer help?

Allan C Jones
Newport Pagnell
Buckinghamshire

Relatively satisfactory

It is true that critics have perceived flaws in the theories of relativity, but it is still the case that relativity does provide a good explanation of observable phenomena. Ove Tedenstig states (*Letters*, November) that Einstein's theories should be relegated to the "lumber room of failed scientific ideas". But why, when no one has produced a better hypothesis?

Critics of relativity must address themselves to some common observations that are not readily explained by Newtonian physics. For example the motion of Mercury, and the behaviour of high-speed electrons in discharge tubes. If relativity is not the (whole) answer then can we have another hypothesis?

Some people have genuine and well-argued reasons to suspect that relativity is not the whole story, but I suspect that the majority of people who dismiss relativity just cannot cope with what, on the face of it, goes against everyday experience. I am reminded of the occasion where the church refused to believe in the moons of Jupiter.

The establishment may well be represented by some people with narrow-minded, blinkered views, but the tone of Tedenstig's letter suggests that there are such people in both camps.

David Gibson
Leed

Who has the problem?

It is with interest that I read your editorial "History is bunk?" (*EW + WW*, November). I note the change of title from *Wireless World*, but I also note the RF techniques are essential to accurate design of even humble circuits, and in particular the 32bit systems with which I am currently involved, are very sensitive to electromagnetic design - transmission line parameters, for example.

I would even assert that a humble bipolar transistor is a radiation-operated device when it has to be modelled to full accuracy, at least conceptually, as a quantum field device. This is essential for the proper understanding of p-type semiconductor material as containing not holes, but virtual positrons. I am not convinced that I have seen a fully satisfactory analysis of why base stopper resistors work - if anyone remembers the concepts of pre-integrated circuit days.

While I appreciate the preference of your magazine for practice and experiment over high-flown theory, I am not convinced by totalitarian relativism, and I suspect that it is a matter of time before Einstein's fundamentals go the way of Newton's principia, that is into history.

Allan Campbell

Travelling in the mind

Taking up the challenge thrown down by Alan Boswell (*Letters*, October), I would like to join the debate on time machines by asking a question:

Does the unfolding process of the material system depend on the mediation of some kind of agent corresponding to the notion of time as under relativity theory, or does this unfolding merely express the inherent dynamic characteristics of matter itself?

This question, raised over the nature of time as it may be inferred from relativity theory, stands in relation to the alternative hypothesis which posits time as an element of the mental domain, the indispensable concept for any mental comprehension of experience.

Should this hypothesis prevail, it follows from the exclusion of time from the physical domain, that timing operations would be admissible only as actions of the mind, when comparisons are made between stages of various physical processes.

Any process adopted as a standard for comparison derives its value from confidence in the qualities of the system undergoing it, to provide a repetition of stages which is regular.

The clock is such a system which the mind uses as a basis for recording the various series of events along an abstract dimension,

but is merely represented as a spatial extension and has no location in the physical universe.

The timing standard has validity across the entire universe and cannot be affected by physical action such as mobility of objects. There are various practical problems in establishing simultaneity, including the finding of data-transmission delays between the site of an event and a timing-station registering it. These difficulties have no bearing on the concept of simultaneity, as Einstein asserted they did. What is measured with clocks is not time, but the synchronisation between processes.

The proposition I am putting is consistent with the Cartesian doctrine of duality: the physical and mental domains are recognised as having their autonomous existences, but their processes are mediated through the action of the neural complexes of living organisms. At this interface is defined the boundary between physics and metaphysics, the boundary which relativity theory vainly seeks to breach.

Am I a kill-joy for trying to undermine the basis for fun with time-machine fantasies and the like?

Possibly Mr Boswell would care to lend his incisiveness, or venture a little crankiness, in a "respectable" debate over the place of time in the universe.

C Francksen
Farnborough
Hants

REGULARS

CIRCUIT IDEAS

Four channels on a single-channel oscilloscope

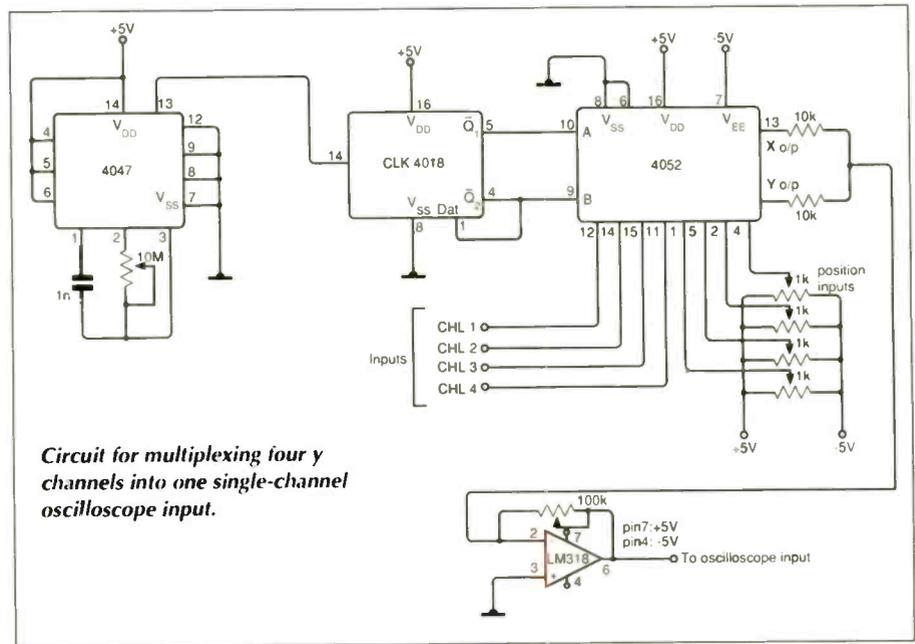
On a single-channel oscilloscope, this circuit, using only four ICs, multiplexes four signal channels for, effectively, simultaneous display.

The differential 4052 multiplexer works with two sets of four inputs: pins 11, 12, 14 and 15 carry the y signal, while pins 1, 2, 4 and 5 take DC potentials from the four potentiometers to determine the y position on the screen (a DC-coupled oscilloscope is assumed).

Clock pulses variable up to 2MHz are generated by the 4047 astable and drive the 2-bit Johnson counter, which produces A and B select waveforms for the multiplexer. High switching rates multiplex the y inputs at a higher rate than the oscilloscope sweep to give a virtually continuous display.

Output to the single input of the oscilloscope comes from an LM318 variable-gain op-amp.

V Lakshminarayanan
Centre for Development of Telematics
Bangalore, India



Accurate astable multivibrator timing

In the free-running multivibrator of Fig. 1 the period is theoretically given by $T = 2CR_1 \ln(1 + 2R_2/R_3)$, positive and negative excursions being exactly equal.

Symmetry of the output waveform suffers in practice when the differential input voltage exceeds the specified value and, in some types of op-amp, causes an avalanche input current. This usually happens as a

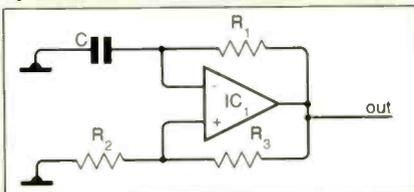


Fig. 1. Commonly used multivibrator circuit may give asymmetrical output if inverting input avalanches.

result of exceeding input threshold protection or when long-tailed pair base/emitter zener action occurs.

Figure 2 shows an improved circuit, in which the unity-gain buffer IC₂ isolates the timing circuit from the inverting input of

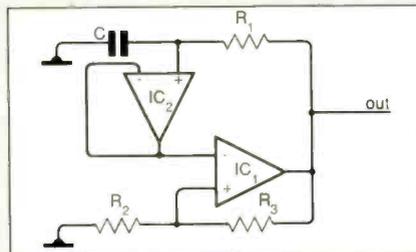


Fig. 2. Modified circuit isolates timing components from inverting input to preserve symmetry.

IC₁, incidentally affording increased speed. Alternatively, the potential divider R_{2,3} may be varied to give a lower differential input swing, but in this case the op-amp offset voltage cannot be neglected.

Dmitri Danyuk and George Pilko
Kiev, USSR

FRESH IDEAS

While we are not short of Circuit Ideas to publish, it would be agreeable to see some fresh input from the vast, untapped bank of talent that our thousands of readers represent. We pay a moderate fee for all ideas published. So send them to Circuit Ideas, EW+WW, Room L333, Quadrant House, The Quadrant, Sutton, Surrey, SM2 5AS.

We will be happy to consider them.

Millihertz multivibrator

When accurate and repeatable long-period timing is needed, a CD4053 analogue multiplexer and a CD4020 14-stage counter will form an astable multivibrator with independent setting of mark and space from seconds to minutes. No expensive large-value, low-leakage capacitors are needed and there is no initial

pulse error, often present in analogue timing circuits.

Analogue switches B and C of the 4053 are arranged as inverter gates, inputs and outputs therefore being complementary. Capacitor C_1 and resistors $R_{A,B,C}$ form an oscillator round the gates.

Pulses from the oscillator are counted by

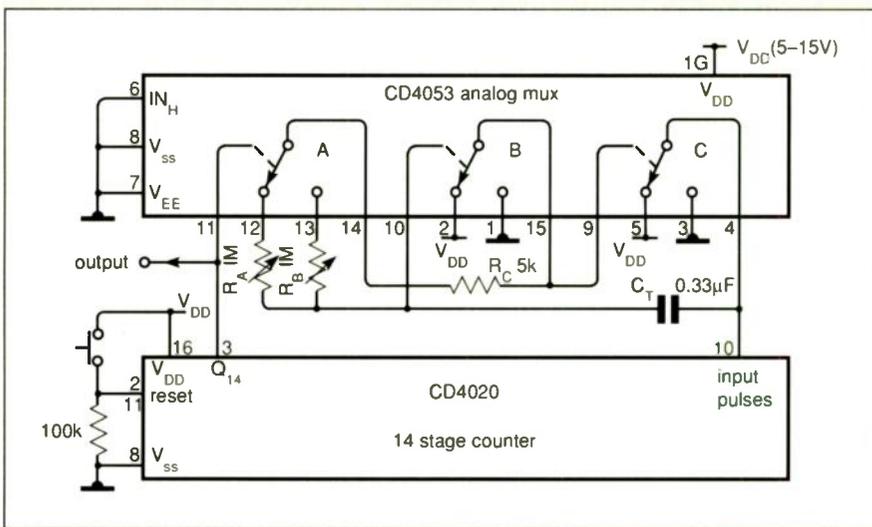
the 4020, its Q_{14} output changing state after every 8192 pulses at the input and controlling, by way of gate A, which of the two timing resistors R_A or R_B is in the oscillator circuit. The frequency of the oscillator is so decided by the value of R_A when Q_{14} is low and by R_B when it is high, Q_{14} being taken as the output.

With the component values shown in the diagram, on and off times are variable between 10s and 70min. Leakage in the off channel of gate A causes negligible change in the timing of each period when the timing resistor of the other period is varied.

If the preset feature of the 4020 is not needed, a 4045 21-stage counter can be used to give longer periods.

M S Nagaraj
ISRO Satellite Centre
Bangalore
India

Low-power counter and multiplexer give independent control of on and off periods of multivibrator from 10s to 70min, using no expensive capacitors. Timing is much more accurate and repeatable than in analogue timers.



Variable M:S op-amp oscillator

Needing a low-frequency oscillator to give a rough idea of the level of a control voltage, I considered the obvious 555 but, having a spare op-amp, developed this variation of a common design.

Op-amp oscillators commonly take the form shown in Fig.1, in which R_1 and R_2 provide positive feedback and the reference voltage. Capacitor C charges through R_3 to

the reference level, whereupon the output goes low and C then discharges to the new level. When C reaches it, the output again goes high and the cycle repeats. With equal supplies, the mark:space ratio is 50:50.

In Fig.2, a single supply is used and the low impedance of the control voltage source enables it to be used to vary charge and discharge times by changing the switching

point of the op-amp to alter the M:S ratio.

Values given provide a led flashing rate of 3Hz, assuming a low-leakage C , and M:S ratio is variable from 3:1 to 1:3 for a control voltage swing of +2V to +10V. I used a low-current led to 0V, but a higher-current device could be driven by a transistor.

Martin J Barratt
Reading, Berkshire

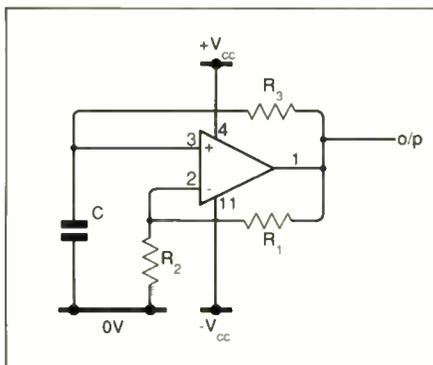
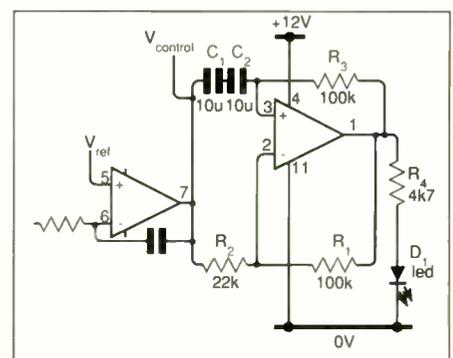


Fig. 1. Common form of op-amp oscillator, providing 50:50 mark:space ratio with equal supplies. Feedback resistors determine reference voltage.

Fig. 2. New circuit with single supply. Control voltage to be monitored varies mark:space ratio of waveform driving led indicator



Parallel-to-RS232-C conversion

The circuit shown in Fig. 1 converts parallel 8-bit data at the inputs of the uart IC₂ (pins 26-33) to RS232-C serial data format for transmission at any of fourteen of the commonly used transmission rates as in Table 1. Data is entered either by means of switches DWS1-DWS8 or from an external source.

Transmission is initiated by applying a positive or negative edge to the trigger signal input of the multiple monostable IC₃, an HEF4528; selection of trigger polarity is by switches TS 1-4. Serial data from pin 25 of the IM6402 uart is inverted and converted to RS232-C levels by the Max232 driver, IC₄, appearing on pin 14. The uart inserts a start bit and either one or two stop bits and odd, even or no parity bits, selected by switches CWS 1-5 as in Table 2. Figure 2(a) shows the data format and Fig. 2(b) the timing.

If data is to come from an external source (for example, from the motion detector published in *EW + WW*, July, pp. 571, *Circuit Ideas*), the switch/resistor network on pins 26-33 of the uart is omitted. In this case, valid data must be present at least 50ns before and 70ns after the trailing edge of the negative pulse at pin 23 of the uart.

K Kumaran
University of Keele

Fig. 1. Parallel-to-RS232-C converter for external data or for switched-input setting.

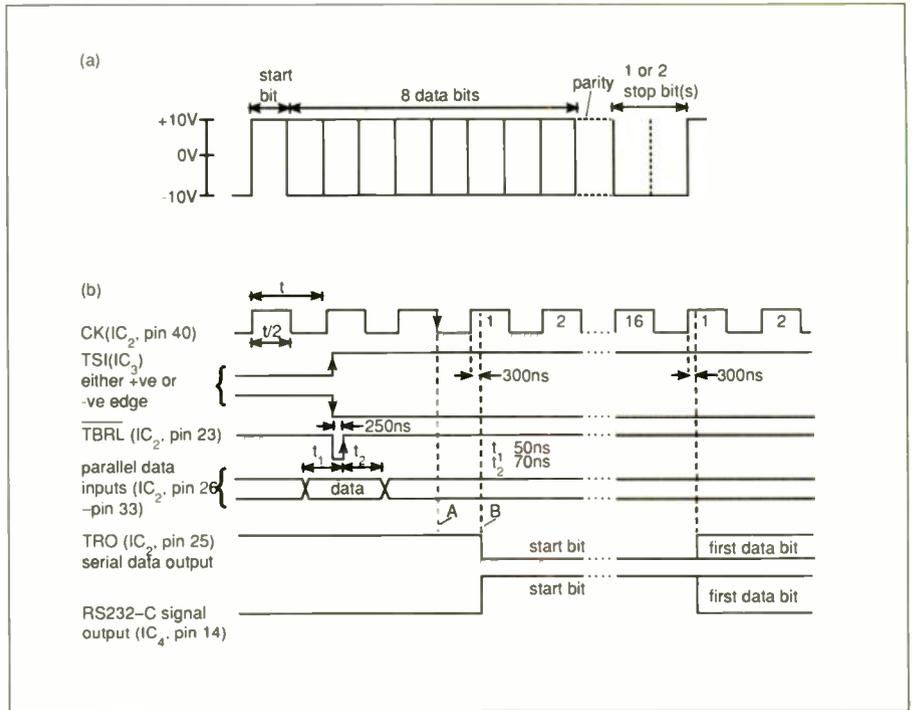


Fig. 2. Serial data format and levels at output of RS232-C driver (a). Number of stop bits is optional, as is inclusion of odd or even parity bit. Timing of circuit is at (b). Point A is first negative edge of clock, at least $T/2+175ns$ after positive edge of TBRL; B is start bit time, $T/2+300ns$ after A.

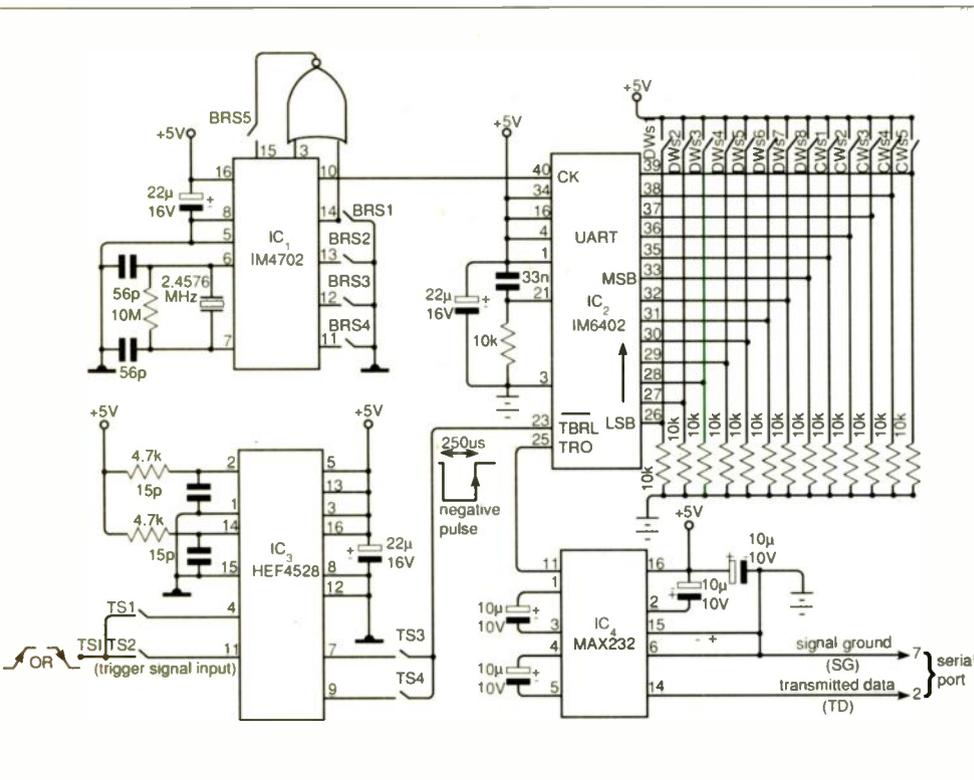
Table 1. Selecting data rate by setting of switches BRS 1-5.

Rate	BRS1	BRS2	BRS3	BRS4	BRS5
50	on	off	on	on	off
75	off	off	on	on	off
110	off	off	off	off	off
134.5	on	on	off	on	off
150	on	off	off	off	off
200	off	on	off	on	off
300	off	on	off	off	off
600	on	off	off	on	off
1200	off	off	on	off	off
1800	on	off	on	off	off
2400	on	on	off	off	off
4800	off	on	on	off	off
9600	on	on	on	off	off
19200	off	off	off	off	on

Table 2. Selection of start, stop and parity bits.

CWSC	WCS	CWS	CWS	CWS	Parity	Stop bit(s)
1	2	3	4	5	x	none 1
on	off	on	on	x	none	2
on	on	on	on	x	none	2
off	off	on	on	off	odd	1
off	on	on	on	off	odd	2
off	off	on	on	on	even	1
off	on	on	on	on	even	2

x = don't care



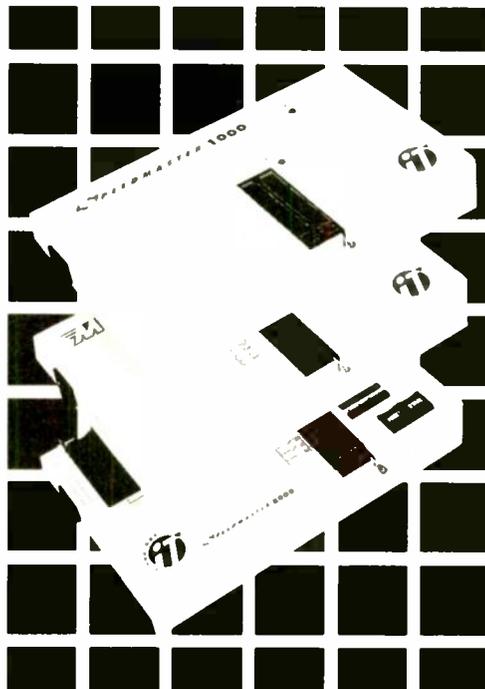
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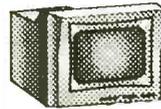
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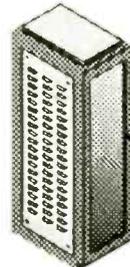
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Triple-metal masters. Two triple-metal masters have been added to the TC160G series of gate arrays. These achieve maximum usable gate counts of 210,000 using 0.8 μ m hc²mos technology. The usable gate figure is based on 70% gate utilisation compared with 40% for double-layer metal masters. The arrays are supported by a library of about 1000 macrocells as well as megacells for ram and rom. Toshiba Electronics, 0276 694600.

A-to-D & D-to-A converters

10bit. The SPT7820 and SPT7824 monolithic 10bit converters have sampling rates of 20 and 40Msamples/s respectively. They are suited to medical and industrial imaging and have TTL compatible inputs and outputs. There is a fully integrated track and hold on the same monolithic die whereby input signals of up to 10MHz can be sampled. Ambar Cascom, 0296 434141.

12bit. The AD7233 and AD7243 12bit converters are for process control, calibration circuits, DSP based systems, and general I/O subsystems. With an internally connected 5V reference, twos-complement data format, and single output range of $\pm 5V$, the AD7233 is suitable for bipolar zero-centred process control applications. It can have internal or external reference connections, offset binary or twos-complement data format. Analog Devices, 0932 232222.

8bit. The DAC8840 and DAC8841 TrimDacs are 8bit octal multiplying D-to-A converters for replacing mechanical potentiometers for automatic microprocessor adjustments of AC and DC voltage gain. Eight independent channels of

digitally programmable signal-level attenuation provides 256 values of unipolar or bipolar gain (two or four quadrant multiplications) for DC to 1MHz analogue signal inputs. Each buffered channel can provide a minimum 5mA of output drive current. Analog Devices, 0932 232222.

12bit. The HI5800 is a 3Msamples/s 330ns 3MHz monolithic 12bit A-to-D converter. The 10,000-transistor chip has an on-chip voltage reference and sample and hold that samples below 1 μ s and converts above 1MHz. Distortion is 72dB. It contains a buffered sample and hold amplifier, precision temperature and curvature corrected bandgap voltage reference (2.5V ratio metric), two-step subranging A-to-D with 7bit flash and 7bit D-to-A with digital error correction, control logic, and timing generator. It can also be driven by a 2.5V external reference. Harris Semiconductor, 0276 686886.

Linear integrated circuits

Battery back-up. Battery back-up IC S8420 has been added to the Seiko range of low power linear ICs. It is for switching circuits of main and back-up power supplies in hand-held or battery powered equipment, and consists of a voltage regulator, three voltage detectors, a power alteration switch, and a control circuit. Amega Electronics, 0256 843166.

Audio preamp. SSM2017 integrated microphone preamplifier replaces discrete solutions made from up to 20 passive components, four transistors and an op amp. It is housed in an 8-pin minidip and needs a resistor for setting gains between unity and 1000. Input noise is specified at 950pV \sqrt{Hz} at 1kHz. Total harmonic distortion is typically 0.01% from 20Hz to 20kHz at 100 gain. Output signals of 100V RMS can be driven into low load impedance without significant degradation of performance. Analog Devices, 0932 232222.

Bipolar op amps. OPA177 and OPA77 precision bipolar op amps have laser trimmed offset, drift and input bias current. Input offset voltage is 4 μ V typical, 10 μ V maximum, at 25°C, with minimum drift specified at 0.1 μ V/°C across the -40 to +85°C range. Typical unloaded power consumption is 40mW and typical input bias current 0.3nA. Open loop gain is 134dB minimum and common mode rejection ratio is at least 130dB. Noise voltage is 85nV RMS referred to the input, and closed loop unity-gain bandwidth is typically 600kHz. The inputs are protected against up to

$\pm 30V$ differential inputs by 500 Ω series input resistors and diode clamps. Burr-Brown International, 0923 33837.

Feedback amp. A precision voltage feedback amplifier, the EL2075, has a 2GHz gain-bandwidth product, settling time of 13ns to 0.1%, and a minimum of 50mA output drive current over temperature. It is gain-of-ten stable with a -3dB bandwidth of 400MHz at an Av of +10. Input offset voltage is 200 μ V and input bias current 2 μ A. It is available in 8-pin dip, eight-lead SO, and 8-pin military cerdip. Elantec, 071-482 4596.

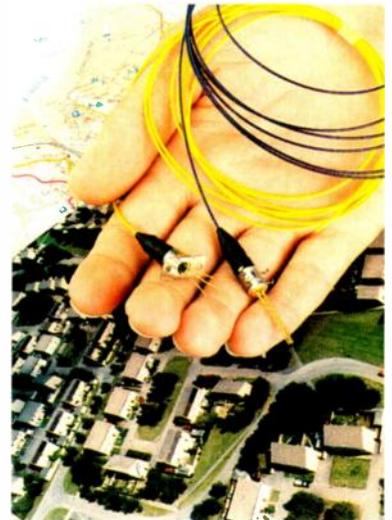
Monolithic amp. EL2044 is a monolithic amplifier, operating from a single 2.5V supply. It is designed to drive low impedance loads where it can drive a 6V peak-to-peak signal into a 150 Ω load. It can also drive unlimited load capacitances and, because of its conventional voltage feedback topology, can be used with reactive or nonlinear elements in its feedback network. It is unity gain stable and has a 325V/ μ s slew rate and 60MHz gain-bandwidth product. Elantec, 071-482 4596.

Supervisory circuit. A microprocessor supervisory circuit includes a conditional battery back-up feature for ram data and has a guaranteed reset assertion down to 1V, preventing microprocessor malfunction at low supply voltages. Chip enable gating on the LTC1235 is 35ns maximum and supply current is 1.5mA maximum. It is supplied in a 16-pin SO or dip package. Linear Technology, 0932 765688.

Battery-charger IC. U2400B offers three programmable charging times of 30min, 1h or 12h with subsequent automatic trickle charging. It also provides an automatic predischARGE facility for NiCd cells to ensure complete discharge before recharging. Two independent charging interrupts protect batteries from damage due to overvoltage and over-temperature conditions. An integral PWM comparator ensures batteries of different capacities can be accommodated. Telefunken Electronic, 0635 30905.

Memory chips

2Mbit sram. 8F8259C 2Mbit cmos sram is organised as 256K by 8bit. It is based on two 256K by 4bit srams mounted on a multi-layered epoxy laminate FR4 substrate and has access times from 20 to 55ns. The 32-pin 0.6in DIP pinout adheres to the Jedic standard. All inputs and outputs are TTL compatible and



In the hand: Harris' laser diode and photodiode.

operate from a single 5V supply. Electronic Designs, 0276 72637.

32Kbit fifo. PDSP16540 fifo, configured as 1K by 32bit, is designed to extend capabilities of the PDSP16510 FFT. It can be used as a flexible data reservoir in any DSP system. Up to 40MHz data read and 16MHz data write rates can be sustained. Words, read as a complete block, can be programmed in multiples of 32 up to a maximum of 1024. GEC Plessey Semiconductors, 0793 518000.

128bit eeprom. X24C00 is a 128bit cmos serial eeprom organised as 16 by 8bit and made by Xicor using textured poly floating gate technology. It has a serial interface and software protocol allowing operation on a two-wire bus at a 1MHz clock rate. Available in an eight-pin minidip or SOIC package at commercial and industrial temperature ranges. Micro Call, 0844 261939.

1Mbit dram. The MT4C4256H is a 3.3V low-power extended refresh dram in a 256K by 4bit configuration. It is aimed at the 3.3V flat-panel controllers used in low-voltage laptop and notebook computers. Typical standby current is 0.1mW and typical active current is 100mW. Refresh rate specification is extended from 8 to 64ms. Low battery back-up current has a maximum specification of 90 μ A. Micron Technology, 0344 360055.

16Kbit fram. Ramtron FM1408 ferroelectric ram, organised as 2K by 8bit, gives equal read and write cycle times with 150ns maximum read

access. From a single 5V supply it consumes 44mW operating and 55µW standby. All input and output pins are CMOS/TTL compatible. Standard 28-pin package. Pin one switches between dynamic and nonvolatile modes. Mogul Electronics, 0732 741841.

1Mbit sram. Three families of 1Mbit srams including versions with 12ns access times are based on 0.7µm microlithographic technology and have a bicmos structure. They are available in single-outline J-lead and DIP packages. TC55B4257 is a 32-pin 256K by 4bit unit; TC55B4256 is a 28-pin 256K by 4bit unit, and the TC55B812 is a 32-pin 128K by 8bit unit. Toshiba Electronics, 0276 694600.

Microprocessors and controllers

Z80 Microcontroller. FEM180 microcontroller, incorporating the Z80180 CPU, offers an interface providing 48 digital I/O lines and three serial ports, 32K sram and 32K eprom. It comes with a firmware monitor for program development using a PC or dumb terminal. FES180 support card has PSU, 24 8mA drivers, six 5mA drivers, DPCC relay, and space for two extra cards. RS232, RS485 and 20mA current loop interface circuits provide communications. Fernwood Electronics, 04917 8898.

8bit microcontroller. OLMS65K single-chip 8bit microcontroller has internal rom capacities from 4 to 64Kbyte and external memory capability of 64Kbyte. Instruction cycles are 400ns with 10MHz clocks and current consumption is typically less than 25mA. Most devices in the family have 16bit capture and compare registers for high precision timer measurements and one device has an 8bit eight-channel A-to-D converter. Highland Electronics, 0444 236000.

Optical devices

Laser and photo diodes. HL1325CF laser diode and HR1105CF photodiode operating temperature range is -20 to +70°C. The laser diode consists of a 1.3µm Fabry-Perot diode in a miniature coaxial package with a single-mode fibre pigtail. It gives a kink free optical output of 0.3mW at ambient 70°C. Photodiode is an InGaAs pin unit in a miniature coaxial package with a multimode fibre pigtail. Photosensitive aperture is 80µm. Optical sensitivity is 0.78A/W at 1.3µm. Hitachi Europe, 0628 585000.

SM led. A high brightness surface-mount led, called Topled, based on the Tantal-B capacitor package, incorporates an internal reflector to



In the rocks: OLMS65K 8bit microcontroller from Highland Technology.

increase the on-axis brightness to a level comparable with standard leaded leds. Colours are standard red, orange, yellow, green and hyper red. Versions are also produced using single and double heterojunction GaAlAs die giving high brightness red leds with typical on-axis intensity of 20mcd at 10mA, emission half angle of ±60°. Siemens, 0932 752323.

Laser diode. SLD1301XT visible laser diode has an optical output of 100mW and a nominal wavelength of 670nm. It comes with a thermoelectric cooler and thermistor housed in a 20 by 33mm flat package. 2.5V drawing 600mA under typical operating conditions. Typical threshold current is 450mA. Temperature range from -10 to +30°C. Sony Components & Computer, 0784 466660.

Programmable logic arrays

PLA pair. Two programmable logic array devices are claimed to match the speed of the fastest PAL chips without the architectural limitations of current PAL parts. With propagation delays of 10ns, the Plus153-10 and 173-10 are for high speed I/O and memory address decode functions in PCs and workstations as well as memory and address mapping applications, specialised arithmetic functions, code conversions, and data manipulation. Signetics, 0101 408 991 2000.

Power semiconductors

SCSI regulator. LT1117-2.85 is a 2.85V low drop out regulator for use in active terminations for the SCSI standard. It provides a regulated output of 2.85V ±1% from the SCSI termpower supply. Output current is 800mA. It comes in a SOT223 package and operates down to 1V drop out voltage. Quiescent current is 10mA maximum. It handles fault conditions with short-circuit current limiting, thermal shutdown, and on-chip ESD protection. Linear Technology, 0932 765688.

Quad drivers. Two quad RS485 drivers have maximum supply currents 300 times lower than earlier RS485 drivers. The LTC486 is a pin-compatible replacement for the SN75172, DS96172 and 96F172. And the LTC487 replaces the SN75174, DS9G174 and DS96F174. They draw a maximum 200µA of supply current and support data transmission rates up to 10Mbaud. They operate from a single 5V supply and can handle -7 to +12V common mode range on the bus. Linear Technology, 0932 765688.

Power IC. The TPIC2801 is a monolithic intelligent power IC with eight 1A/30V outputs each configured as a low side switch. The eight switches are controlled from a single input by an 8bit serial word. Each of the eight drivers in the 30V device has a 40mJ rating and can drive up to a 30V 1A load. The presence of a 35V collector base clamp on each switch eliminates the need for external clamp diodes when switching inductive loads. Texas Instruments, 0234 223252.

Quad driver. The TPIC2404 is a monolithic quad 1A low side driver for switching peripheral loads such as relays, motors, solenoids, and other loads requiring up to 45V supply voltage. Each of its four 1A power outputs has overvoltage, over-temperature, and current limiting protection. It comes in a 15-pin 25W sip and is specified for the -40 to +125°C range. Texas Instruments, 0234 223252.

Quad mosfet. The TPIC2406 quadruple mosfet latch is for high power load applications and contains four self-protecting low-side switches with output clamp diodes for inductive transient protection. Each open drain output can drive a continuous output current of 700mA while operating from voltages as high as 60V. Pulsed current outputs up to 3A per channel are possible because of the 0.5Ω driver output resistance. It can also be cascaded to deliver a peak output current of 12A. Texas Instruments, 0234 223252.

PASSIVE

Passive components

Ceramic caps. The Capax parallel plate ceramic microwave capacitors are designed for minimum insertion loss at frequencies up to 40GHz. They range in size from 0.01 by 0.01in to 0.1 by 0.1in with a thickness of 0.005in for 50V and 0.007in for 100V DC specification. There are 14 standard dielectrics available and capacitances range from 0.05 to 1500pF. They work from -55 to +125°C. Anglia Microwaves, 0277 630000.

Voltage suppressors. Ten passive devices, with maximum continuous voltage ratings from 3.5 to 69V DC, have been added to the ML multilayer series of surface mount transient voltage suppressors. Applications include logic protection (3.5 to 5.5V), automotive (14 to 18V), computer communications such as RS232 (26V), and telecom line cards using high voltage DC analogue (33 to 68V). As well as being fully bidirectional, they are up to six times smaller than Zeners and need no derating for operation at 125°C. Harris Semiconductor, 0276 686886.

Electrolytic caps. For use in switching power supplies, the PQ series of electrolytic capacitors has a load life of 160,000h at 55°C. Impedance is 0.16Ω minimum and temperature range is from -55 to +105°C. Working voltage range is 6.3 to 50V DC and capacitance range from 0.47 to 390µF, ±20% tolerance. Allowable ripple is 460mA maximum and leakage current 4µA. The radial lead units range in size from 5 by 1mm to 8 by 11.5mm. Nichicon, 0276 685393.

Electrolytic caps. For Hi-Rel and high ripple current (2.1 to 30.5A) applications, the NR series of electrolytic capacitors has a load life of 40,000h at 55°C. The screw terminal units have can sizes from 35 by 80mm to 90 by 190mm, operating temperatures from -40 to +85°C (16 to 100V) and -25 to +85°C (160 to 450V), capacitances from 470 to 470,000µF, tolerance 20%, and leakage current 5mA. Nichicon, 0276 685393.

Current limiters. Added to the NTC surge protector range are 13mm diameter metal oxide in-rush current limiters. They are available with cold resistances of 5 to 16Ω and with steady state currents of 3 to 5A. Applications include halogen lamps and transformers. Power Development, 0823 335200.

Connectors and cabling

IDC connectors. The UL approved Harting SEK18 series of IDC flat cable connectors have from 6 to 64 contacts. The male headers have angle and straight pins in lengths of 2.9, 4.5 and 15mm. Grid pattern for the male connector is 2.54mm and for the female 1.27mm. Current rating is 1A, contact resistance 20m Ω , and operating temperature -55 to 125°C. Gothic Crellon, 0734 788878.

Zif connector. A compact zero insertion force connector is totally self contained with no manual actuation mechanism. Called DL Drawer, it uses the movement of the drawer or subassembly to mate and unmate the connector halves. It has been tested to withstand 100,000 mating cycles and comes with crimp contacts, wire wrap or solder tails. It can be used for PCB, cable or flat-flex terminations and uses gold over nickel plated copper alloy contacts. ITT Cannon, 0256 473171.

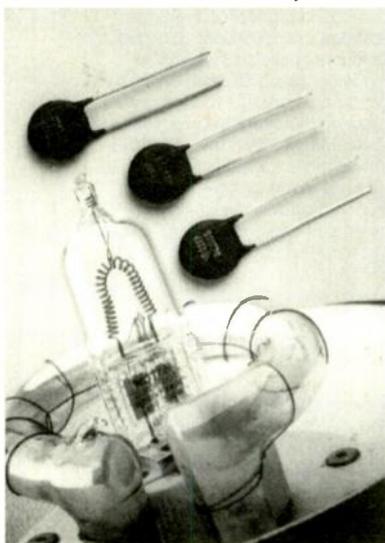
Displays

Plasma display. The FPF8050HRUC-001 is a 10in AC gas discharge plasma display with a 640 by 400pixel resolution matrix with dots of 0.33mm pitch. Typical brightness is 150cd/m², contrast ratio exceeds 20:1, and viewing angle is 160°. Service life without reduction in brightness is 50,000h. It can be used as a flat-screen CRT replacement or in infra-red touch sensitive screen overlay systems. Fujitsu Microelectronics, 0628 76100.

Hardware

PC chassis. The Armagard Pro-chassis lets custom computer

In the rush: NTC inrush current limiters from Power Development.



systems be built using IBM PC compatible motherboards and backplanes. It comprises an outer enclosure, front and rear card supports, shock-proof card clamps, and ventilated disc drive housings for 3.5 and 5.25in drives. Minor panel work will allow ticket printers, keypads and screens to be incorporated. It can be desk or 19in rack mounted. Intek Electronics, 0352 85603.

Fan. The Shicoh 0410N-12 40 by 40 fan is 10mm deep and delivers 4.24cfm at a noise level of 26dB. It has UL approval for flame resistance and class E insulation. The DC brushless axial fan also has full protection against burn-out and short-term polarity reversal. It works from a 12V DC supply, consumes 1.08W, and has a 30,000h life span. Key Electronic Components, 0734 351546.

Instrumentation

Analogue multimeter. The Circuitmate AM12 analogue multimeter uses fet technology to prevent loading the circuit under test thus giving error free readings. It incorporates a 115mm mirror scale for parallax-free readings and RMS, peak-to-peak and dB scales are provided for AC voltages. A centre-zero scale and adjustment is provided for AC and DC voltage measurements. AC and DC current and voltage measurements are to 12A and 1.2kV. Beckman Industrial, 0384 442394.

RF wattmeters. The ThruLine range of 2 to 1000MHz 250W to 250kW \pm 5% wattmeters are rectangular 4 by 4.5in multiscale glass plate meters with 50 Ω line section and 10ft of shielded interconnect cable. The carrying case provides storage sockets for extra plug-in items. They are also available as panel meters for 19in rack mounting. Bird Electronic, 0101 216 248 1200.

50MHz scope. The 50MHz V525 and VC6024 are combined real-time and digital storage oscilloscopes. The portable V525 is mainly operated with DC offset and alternative magnifier functions. Stable triggering is possible on both channels even if the channel frequencies differ. The VC6024 has a repetitive signal sampling rate of 20Msample/s, two channel alternate, or 100Ksample/s, two channel chopping. Memory capacity is 2Kword on both channels at 50 μ s/div to 50s/div and 1Kword at 50ns/div to 2 μ s/div. Hitachi Denshi, 08 202 4311.

200MHz scope. The 200MHz 100Msample/s (four channels simultaneously, memory capacity 8kW/channel) VC9140 digital storage oscilloscope incorporates a PC which is FDD compatible with PC-Dos. The



In the slot: Armagard Pro-chassis from Intek.

9in gas plasma flat display has PC equivalent menus and submenus that are displayed at all times. Up to 17 waveform parameters can be observed with plus, minus and multiplication operation between waveforms, waveform inversion and absolute value operations. Special trigger facilities are provided. Hitachi Denshi, C81-202 4311.

RMS/peak voltmeter. The URE3 RMS/peak voltmeter is designed for taking measurements in environments that are subject to severe interference and high electromagnetic fields. It is also suitable for use in EMC laboratories and for materials testing. It has passed IEC and VDE tests with only minimal problems and all the disturbances visible during operation disappeared as soon as the source of the interference was removed. Neither the instrument set-ups nor the readouts underwent lasting change. Rohde & Schwarz, 0252 811377.

GPIB scope. The 3100D digital storage oscilloscope from Leader is controllable via a GPIB interface. It can sample at 40Msample/s with storage of waveforms up to 100MHz. Vertical resolution is 8bit, 256 points, and horizontal 11bit, 2048 points. Each channel has a separate reference memory allowing the storage of up to four waveforms. A summation facility allows 256 acquisitions to be averaged. Thurlby-Thandar, 0480 412451.

Literature IC selector guide. Motorola has revised its linear and interface ICs selector guide and cross reference - SG96/D revision 4. The 112-page guide includes switching regulator control circuits, RF communication circuits and surface mount devices as well as a variety of the previous standard devices. Motorola, 0908 614614.

Production equipment

Soldering irons. A range of antistatic soldering irons has been designed for hand soldering static sensitive devices without damaging the components. Any charge built up on the tip is earthed through the handle and lead. The lead is made of a carbon loaded silicone rubber compound and the handle a carbon fibre-reinforced thermoplastic material. The 240V AC model has a tip temperature of 410°C and comes with 2m cable and standard 4.8mm diameter chisel bit and hook. The 24V AC model can have tip temperatures from 350 to 500°C and comes with 1.25m cable and 2.4mm iron-plated bit. RS Components, 0536 201234.

Power supplies

1kW switcher. The 9C series of 1kW switching power supplies has 5, 12, 15, 24, 28 and 48V single outputs and is approved to IEC950, UL1950 and CSA22.2 requirements. Built-in features include an EMI filter to FCE/VDE level A, soft start inrush current limiting, single-wire parallel current sharing, input power fail and output good signals, remote adjustment and margining, and overvoltage and thermal shutdown protection. It measures 5 by 5 by 10in. Astec Standard Power, 0246 455946.

1kW supply. With universal 90 to 264V AC input range, 0.99 active power factor correction to meet IEC555-2, and better than 75% efficiency, the BVM10000 1kW power supply has four output configurations in a 305 by 203 by 86mm ventilated case. Power density is more than 3W/cu in. Outputs of 5V/150A, +12V/20A and -12V/10A are common to all models. The fourth output can be 3.3V/10A, 5V/10A, 12V/10A or 24V/5A. Input surge current is limited

to 30A. Operating range is 0 to 70°C with full power derating linearly to 50% from 50°C. BICC-Vero Electronics, 0489 780078.

DC-DC converters. A series of PCB mounting low-profile DC-DC converters comprises isolated modules for use in decentralised power systems. Called PKE, these units are rated from 25 to 30W and are aimed at the telecomms and data communications industries. They can operate continually with natural convection cooling and run directly from 48 or 60V battery systems. There are five models in single, dual and triple output versions, and all have a 10.7mm profile and a 3 by 3in footprint. Ericsson Components, 0203 553647.

Uninterruptible supply. The Accupower Gold UPS from Emerson complies with IEE555-2 and is aimed at PC lans, multi-user systems, printers, phone systems, laboratory equipment, epos, and process control. Two ratings are available - 1kVA (AU1000) and 1.5kVA (AU1500). Gardners Transformers, 0202 482284.

Triple supply. The Model 1300 bench power supply has triple floating outputs and short circuit protection. The first output is 5V variable from 0 to 1A with current limiting and displayed on an analogue meter with a ±5% accuracy. Regulation on line is 0.2%, load 1% and maximum ripple 10mV. The second and third outputs are variable from 0 to 20V with a maximum current of 0.25A. Regulation is 0.05% for line and 0.1% for load. Ripple is again 10mV

In the light: 386SX processor board from Arcom.



maximum. Global Specialties, 0978 853920.

Uninterruptible power. The Delta series of uninterruptible power supplies are rated from 3 to 17.5kVA and are fitted with an interface that can automatically initiate an orderly shutdown of a computer system before the UPS batteries are exhausted during a mains failure. They are compatible with IBM AS/400 and several other mini and mainframe computers as well as major network systems. They support crest factors of 5:1 without derating and offer back-up times from 30min. Victron, 0455 618666.

DC-DC converter. The NFC20 from Computer Products is a 20W output DC-DC converter housed in a 2 by 1.6 by 0.4in package. It has input voltage ranges of 18 to 36V and 36 to 72V, five output voltage variations, and an MTBF of one million hours. With no heatsink required and no derating up to 60°C, it uses a switching frequency of 200kHz and offers a 2:1 input voltage range, remote on/off control, and overvoltage protection. XP, 0734 845515.

Radio communications products

Spectrum analysers. Two microwave analysers for digital mobile radio are designed to handle the fast rise time characteristics associated with GSM and PCN. Made by Advantest, the R3265 and R3271 respectively cover the ranges 100Hz to 8GHz and 100Hz to 26.5GHz. Frequency span covers 200Hz to full span with an accuracy of ±3% for spans greater than 25MHz. In zero span, sweep times range from 50µs to 1000s. Plug-in data memory cards are standard on each unit. Chase Electronics, 081 878 7747.

Data receiver. The SL6649-1 is a compact direct conversion FSK data receiver for the radio paging market and contains a low noise RF amplifier for signals up to 200MHz. The signal is split into I and Q channels, following a direct conversion architecture, then into mixers, such that with an external LO they can be mixed down to baseband for on-chip processing. It contains on-chip capacitors for channel filtering and requires the minimum amount of external components to become a single chip receiver, handling RF at one end and providing data at its output up to the maximum paging rate of 1200baud. GEC Plessey Semiconductors, 0793 518000.

Switches and relays

Pushbuttons. A range of PCB or panel-mount alternate-action maintained lighted miniature pushbutton switches is called the LVP/LHP series. Rather than being just back-lit, the whole actuator lights

up. They use silver plated contacts rated at 24V DC, 50mA, and tin/lead plated terminals. Life expectancy is one million cycles at rated load. Solder heat resistance is 260°C/5s. Six versions are available including front-panel mounted, vertical PCB (round and square), and horizontal PCB in normally open or closed options. Augat, 0952 670281.

Encoder switches. Grayhill has introduced a range of optically encoded rotary encoder switches for the audio-visual, aerospace and medical markets. As well as the rotary function, there is a pushbutton element activated via the switch shaft to let a digital code be set and entered. They meet MIL202 for vibration, shock and humidity. All provide quadrature 2bit code output and devices are available with 16 and 32 detent positions. Highland Electronics, 0444 236000.

PCB switches. A family of pushbutton and toggle switches, the Elma Type 09, are for PCB mounting and through panel applications. Either latching or momentary options can be selected for the pushbutton options each offering two n/o contacts switching up to 42V DC and 200mA, 2.5VA switching capacity. The toggle switches can be two or three position. The standard 2.54mm PCB pinout conforms to DIN41494. Radiatron Components, 081-891 1221.

Television components

AV switch. The TA8628N is a monolithic AV switch with electronic volume control. Housed in a 24-pin shrink dip, it can be used in various tv applications such as Scart switches and switching between, say, tv and video recorder. The video section has two inputs and produces monitor and tv outputs. The parallel sound section has left and right sound inputs for the tv and external signals, producing separate tv and audio left and right outputs. Also included are a mute function and sound volume controls for left and right channels. It runs from a 12V DC supply and works from -20 to +70°C. Toshiba Electronics, 0276 694600.

Transducers and sensors

Load indicators. A collection of load indicator and controller systems comprises load cells or load washers and various 3.5 and 4.5 digit LED indicator controllers. Load cells range from 30g to 200tonne. They can be supplied scaled in any variety of engineering units including tonnes, kN and volume capacity. Accuracy varies from 0.1 to 0.5%. Control Transducers, 0234 217704.

Infra-red sensors. Pyroelectric infra-red sensor modules from Seikosha have a low current drain design which includes an amplifier, comparator and

timer on a single circuit board. They are for surface mounting. A light-dependent resistor is incorporated to prevent daylight operation. Minimum operating current is 1mA (3mA maximum) and operating voltage is 5.5V DC. Masking time is 1.2s, circuit stabilising time is 12s typical, sensor rise time is 10s, and operating temperature range is -10 to +50°C. Without a lens, the detection range is 1.5 to 2m. ESD Mercator, 0493 844911.

Pressure transducer. The Autotran-700 transducer has its lowest range at 25Pa (0.25mbar) and can tolerate 100kPa over-pressure. Models from 25Pa to 1.25kPa come as standard. Double ranges are available, for example ±250Pa. Compensated for temperature variations from 5 to 60°C and 1% repeatability standard, the long term drift is not more than 1% a year. EuroSensor, 071 405 6060.

COMPUTER

Computer board level products

Notebook subsystem. OakNote is a notebook PC subsystem with operating system independent power management control that lets makers of notebook and hand-held PCs design a full 25MHz 286/386SX PC motherboard using only three chips. Using OakNote, a 386SX motherboard needs only 34sq in. The three chip subsystem comprises the OTI041 system controller, the OTI042 peripheral controller and the OTI043 flat panel VGA controller. Ambar Components, 0844 261144.

386SX board. The PC386SX is an AT compatible 16 or 20MHz 386SX bus-based processor board for embedded applications. It is aimed at engineers building systems for industrial use. The ScatSX chipset is used and there are 16 memory sites allowing the board to be supplied with up to 8Mbyte of dram expandable to 16Mbyte via a local expansion bus port accepting a plug-on module. Further hardware includes three Flash compatible eprom sockets, 128Kbyte sram, maths coprocessor socket, SVGA controller with 0.5Mbyte of video ram, and a feature control facility for the display of video pictures. Arcom Control Systems, 0223 411200.

Data Acquisition. The PC74 data acquisition board from UEI is for use with PC/XT/AT and PS/2 models 20 and 30. There are 16 analogue inputs accurate to 12bit and a built-in programmable gain amplifier with differential inputs. Either a low or high

gain set of programming gains is available so the user can mix high and low level signals without external signal conditioning. Citadel Products, 081-951 1848.

ADC card. The DB140A is a 12bit 10MHz A-to-D card for use with VME DSP boards based on Motorola and Texas Instruments processors. It integrates all of the components necessary to form a complete data acquisition system on a single 3U VME card. It uses the dBex mezzanine bus for transfers of acquired data, and includes sample rate generation via an on-board 20MHz clock and a fifo up to 4Kword deep for output data storage. Inputs can be from 108mV to 1.024V. Data Beta, 0734 303631.

Single board computer. A 386-based single board computer for PCbus systems from I-Bus uses the 40MHz Am386DX 32bit processor with 128Kbyte of on-board cache. Called I386/40, it is configured as a standard format 16bit AT/ISA card and can support up to 32Mbyte of on-board dram. It is supplied with an IDE hard disc interface and floppy disc controller. Two serial ports and one parallel port are provided as well as a socket for a 40MHz Cyrix CX83D87-40 maths coprocessor. Dean Microsystems, 0734 845155.

Test instruments. A Blue Chip Technology plug-in PCB board offers the facilities of four test instruments - pulse generator, customised waveform generator, universal counter/timer, and function generator - together with IEEE interfaces. The VIP-Gen occupies a single slot of any IBM compatible PC making the PC screen emulate a typical instrument front-panel layout. Test parameters and waveforms can be saved to disc. ESD Instrument Services, 0279 641641.

A-to-D card. By using the 33Mbyte/s DMA transfer rate of EISA computers, AD-Series A-to-D converter cards from Adtek achieve sustained sampling rates of 10Msamples/s at 12bit resolution. Cards in the range go from a single channel 10MHz 12bit resolution to eight channel 200kHz 18bit which is expandable to 32 channels. All have separate converters for each channel, simultaneous sampling of inputs, triggering from a software programmable threshold detector or an external trigger, and an on-board fifo buffer that provides pre and post triggering facilities. Laplace Instruments, 0692 500777.

Computer systems

Notebook computer. The B330SX is a 386SX-based notebook computer using the AMD Am386SXL 25MHz microprocessor. It has a 2.5in 60Mbyte hard disc, 2Mbyte ram expandable to 5Mbyte, triple

supertwist VGA screen with 64 grey shades, 3.5in 1.44Mbyte floppy drive, 80387SX maths coprocessor socket, and optional internal 2400bps modem. Bondwell, 081-365 1993.

Programming hardware

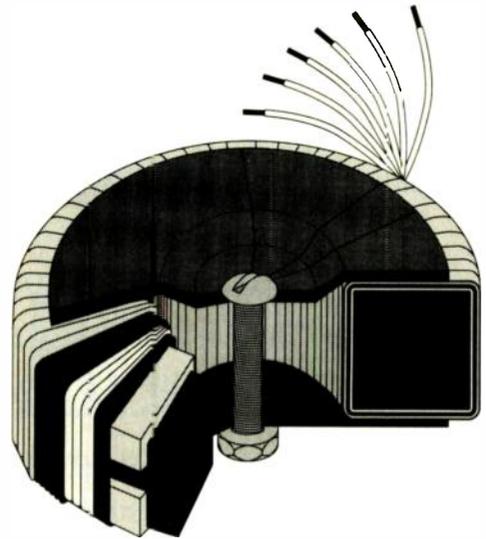
Device programmer. The Tribal Microsystems TUP300 universal device programmer can program pals, gals, peels, FPGAs, serial proms, bipolar proms, e(e)proms, and microcontrollers. The device list supports thousands of devices including the AMD Mach, Altera Max and Signetics 42VA12 series. A facility is also included to test and identify TTL74 and 4000 series logic. Optional gang adapters let it be used as a production tool. Smart Communications, 081-441 3890.

Software

Bus analysis. A software package has been developed to let the Model 4811 bus analyser be remotely controlled from a Macintosh or PC. The analyser performs the functions of a bus monitor, device simulator, bus controller, pattern generator, and bus signal waveform recorder. The use of a computer allows expanded data analysis on a larger screen and the reconstruction of the bus signal waveform. The control panel is displayed on the computer monitor and a mouse can be used to activate the command functions. Amplicon Liveline, 0273 608331.

Asic for risc. Solo 1400 version 3.1.5 is a fully integrated asic design package for Sun SparcStations and Sun 4 workstations. It provides a user-friendly schematic capture program, HDL, multi-level analogue and digital simulator, and automatic place and route program. The Synthesise logic synthesis tool is incorporated to let complex logic functions be designed at a 'high level. ES2, 0344 525252.

Serial communications. The Comio V1.0 serial communications software, supplied as a C and 8086 source function library, is for simplifying the development of C programs to provide interrupt driven data communications with the IBM PC com port. There are read/write functions for single-byte, string and blocked data transfers. All I/O functions operate in no-wait mode. The interrupt driver and I/O buffers are only resident during program execution. Micro SciTech, 0252 625439.



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Circuits, Systems & Standards

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Micropower op amp offers simplicity and versatility

Linear circuits intended to meet the stringent demands of medical and industrial instrumentation, remote data acquisition, and portable equipment must deliver precision at low voltages. A low-power, battery-operated op amp, for instance, requires precision DC characteristics to process low-level signals from high source impedances, low supply current to conserve power, and wide bandwidth to process audio-frequency signals. Because low-voltage applications produce low signal levels, the op amp should have a wide dynamic range at the input and output. Moreover, both it and its external circuit should function properly at the end-of-life battery voltage.

The NE5230 op amp is suited to such requirements. It operates from a supply voltage of 1.8 to 15V and performs well in systems powered by single 5V supplies. The op amp not only offers precision DC characteristics; its common-mode voltage can swing within 100mV of

A little nearer the ideal op amp

As every analogue engineer knows, the ideal op amp would have zero input offset voltage and tempco, zero bias current, rail-to-rail input common mode range, infinite CMRR and PSRR, zero open loop output impedance with rail-to-rail swing and wide bandwidth with high slew rate: they also know that it will not be available in their lifetime, if ever. However, the common mode input range of a few op amps includes the positive rail and in many more (with the popularity of single rail applications) the negative rail. Here is an op amp which includes both and offers a rail-to-rail output swing to boot. IH

either supply rail – a characteristic matched by few other commercially available op amps.

Furthermore, the bias-adjust terminal lets you adjust the op amp's slew rate from 90 to 250V/ms by varying the op amp's internal bias currents. The device also offers decent performance in two other parameters of concern in low-power applications – noise and output-current drive. The NE5230's input voltage noise is 22nV/√Hz at 1kHz, and it can source and sink 5 and 11mA, respectively, when operating from a 1.8V supply at 25°C.

Other key specifications are listed in Table 1. These attributes allow you to use the op amp in battery-powered applications such as half-wave and full-wave rectifiers, window detectors with rail-to-rail input ranges, temperature-limit alarms, sound-activated intrusion detectors, and supply-voltage splitters. An equally important application involves signal-conditioning circuits for bridge transducers – circuits that require no reference voltage or instrumentation amplifier.

Rectify signals without diodes

To keep costs low, battery-operated circuits for consumer applications should have a minimum component count. Fewer components also bestow the bonus of higher reliability. These considerations lead to the half-wave-rectifier circuits of Fig 1.

Neither circuit uses diodes. Because the op amp's input common-mode range extends beyond the supply rails, you can simply ground the non-inverting terminal and thereby configure the amplifier as an inverter. You should also short the bias-adjust terminal (pin 5) to V⁻ to

Table 1. Salient specs for the NE5230 (V⁺=1.8V; V⁻=gnd).

	Bias current	T _A =25°C	0°C<T _A <70°C
Single/dual supply voltage	-1.	8 to 15V or ±0.9 to ±7.5V	
Supply current	low	110µA	250µA max
	high	600µA	800µA max
Output swing	any	1.6V	1.4V min
	any	0.4mV	4mV max
V _{OS}	low	20nA	150nA max
	high	40nA	200nA max
A _{VO}	low	150V/mV	50V/mV min
	high	200V/mV	100V/mV min
CMRR	any	95dB	80dB min
	high	5mA	4mA (typ) at low bias
Output source current	high	11mA	5mA (typ) at low bias
Slew rate	low	90V/ms	90V/ms
	high	250V/ms	250V/ms
bandwidth	low	250kHz	-
	high	600kHz	-

*Note. THE NE5230 operates at low bias current if the bias adjust pin (pin 5) is left open. Shorting the NE5230's pin 5 to V⁻ provides maximum bias current. Connecting a variable resistor between pin 5 and V⁻ lets you adjust the amplifier's bias current and high-frequency characteristics.

Fig. 1. These positive (a) and negative (b) half-wave-rectifier circuits accomplish their job without the use of diodes. The resistors give you the option of gains other than unity.

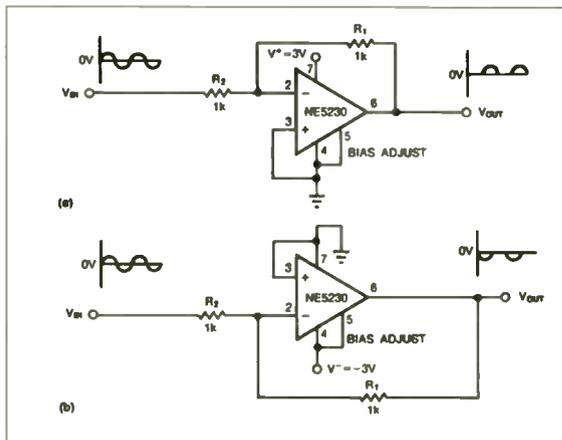
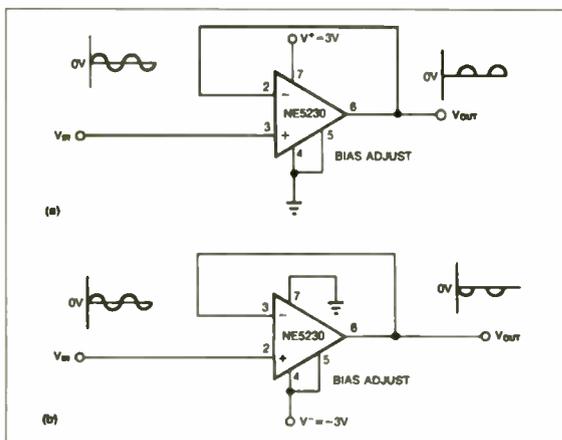


Fig. 2. Requiring no external components, these op amp circuits perform (a) positive and (b) negative half-wave rectification for ground referenced AC signals.



provide a maximum slew rate.

The amplifier behaves as a unity-gain inverter for negative inputs; positive inputs drive the output into saturation (Fig. 1a). But the NE5230's internal detectors prohibit the hard saturation that would occur in most op amps. Recovery from saturation is relatively fast. Operating from a 3V supply, the circuit can rectify signal amplitudes as high as $\pm 2.85V$ at frequencies well above 10kHz. If the input signal has a reference level between 0V and V^+ , you can simply reference the amplifier's non-inverting input to the same level. If required, resistors R_1 and R_2 can provide a gain other than unity.

To obtain a negative-polarity half-wave-rectified signal using a conventional op amp, you have to provide dual (bipolar) power supplies. The NE5230's rail-to-rail input range and near rail-to-rail output range, however, let you achieve this function using a single supply. Simply connect the supply's positive terminal and the amplifier's V^+ terminal to ground, and connect the supply's negative terminal to the amplifier's V^- terminal (Fig. 1b).

The amplifier's common-mode range lets you reference the input signal to the positive rail (ground) by tying the

non-inverting and V^+ terminals together. (You cannot do this with most op amps, and most op amps' output voltage must remain at least one V_{BE} voltage below the positive rail). In short, you can use the amplifier with a single negative supply to condition the signal output from a variety of ground-referenced sensors. Again, if the input-signal reference is a voltage between 0V and V^- instead of ground, you should connect the amplifier's non-inverting input to the same potential.

Overdriving most op amps (beyond the supply rail, for instance) saturates the input stage, causing a phase reversal within the amplifier that can reverse the feedback signal's polarity. Circuitry within the NE5230 prevents phase reversal for inputs as large as 2V beyond the supply rail. This feature allows the amplifiers of Fig. 2 to produce half-wave rectification without external components for input signals referenced to 0V.

In Fig. 2a, the amplifier output follows the input signal above 0V and goes into negative saturation for inputs below 0V, the output clamps near 0V for negative inputs. The circuit as shown can rectify signals of $\pm 2V$ at frequencies above 10 kHz. Inputs below $-2V$ will cause internal phase reversal, however, allowing the output voltage to rise. You can prevent this situation by adding a large resistor in series with the amplifier's input. To obtain a negative-polarity half-wave rectifier, simply reverse Fig 2a's supply-voltage connections (Fig. 2b). Again, this circuit can rectify 0V-referenced signal amplitudes to $\pm 2V$ at frequencies above 10kHz.

Figure 3's circuit performs full-wave rectification using a single positive power supply. When a negative input voltage causes IC_1 to clamp IC_2 's non-inverting input to 0V, IC_1 delivers current through D_1 and R_3 to the signal source. IC_2 acts as an inverting amplifier for negative input signals.

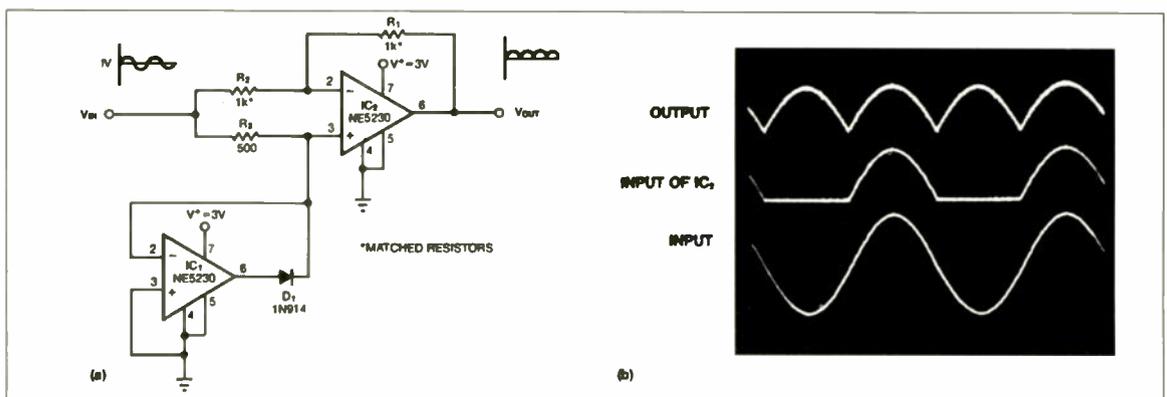
Positive input signals produce a differential voltage between the IC_1 inputs and create reverse-bias across D_1 placing IC_1 's output in negative saturation. This condition removes the 0V clamp at IC_2 's inverting input by breaking IC_1 's feedback loop. Consequently, IC_2 behaves as a follower during positive excursions of the input voltage.

Although D_1 is reverse-biased, clamp diodes at IC_1 's inverting input turn on and draw current through R_3 . Accordingly, R_3 's value should be 500 Ω or less to avoid a significant offset due to this parasitic current flow. (R_1 and R_2 can be large-valued resistors). Figure 3b shows the circuit operating with a 5.7V pk-pk signal at 400Hz.

Similar to the way it rectified the half-wave circuits, the NE5230 performs negative full-wave rectification in Fig. 4 using a single negative power supply. The same precautions apply as for Fig. 3.

You can also use the NE5230 to monitor a signal and to detect fault conditions in which the signal is shorted to either supply voltage. The window-detector circuit of Fig.

Fig. 3. This absolute-value circuit (a) achieves full-wave rectification by clamping IC_2 's non-inverting input to 0V when V_{IN} is negative, and removing the clamp when V_{IN} is positive. Thus IC_2 alternates between an inverter and a follower every half cycle. Photo (b) shows circuit performance at 400Hz for a 5.7V pk-pk input signal. The vertical scale is 2V/div, and the horizontal scale is 0.5ms/div.



5 must have the same supply voltage as that of the remote signal source. Power supply currents through R_1 and R_2 create small offsets essential to the circuit's operation.

Both op amp outputs remain in positive saturation for V_{IN} values between approximately 0 and 3V, which keeps the led off. If V_{IN} shorts to V^+ however, IC_1 saturates negatively (at 0V), turning on the led.

Similarly, IC_2 turns on the led by saturating negatively when V_{IN} shorts to ground. As you can see, the op amp inputs' series resistors and clamp diodes limit the current drawn from the V_{IN} source. Normally, building a two-limit temperature alarm requires a temperature sensor and two op amps. The *NE5230* itself becomes a temperature sensor, however, if you make use of the PTAT (proportional to absolute temperature) voltage at pin 5. This voltage is independent of the supply voltage and measures 14mV at 27°C. What is more, it changes predictably at a rate of 46.667 μ V/°C. For instance, at +85 and -15°C, the pin 5 PTAT voltage is 16.7 and 12.04mV, respectively.

The alarm circuit (Fig. 6) uses these trip points to activate a buzzer when the ambient temperature moves outside the -15 to +85°C window. The R_1/R_2 -divider voltage sets the upper temperature limit and the R_3/R_4 -divider voltage sets the lower one. When the ambient temperature exceeds 85°C, IC_1 's inverting-input voltage is more positive than that at the non-inverting input, and the resulting saturated output (0V) causes the buzzer to sound. Conversely, IC_2 's output sounds the buzzer when the ambient temperature drops below -15°C, again by going into negative saturation.

The resistors that you use in the voltage dividers should have similar temperature coefficients to prevent a shift in threshold voltage as the temperature changes. On the other hand, the op amp's input-offset voltage (V_{OS}) has a greater effect on the circuit's accuracy. Because V_{OS} is a significant percentage of the small PTAT voltage, you must set the temperature limits far apart to reduce error. The typical 400 μ V V_{OS} and 5 μ V/°C V_{OS} drift can introduce an uncertainty of $\pm 15^\circ$ C or more. Although Fig. 6 isn't intended for precision applications, you can improve its accuracy by selecting *NE5230*s with low V_{OS} .

The battery-operated intrusion detector of Fig. 7 illustrates another type of alarm circuit possible with the *NE5230* op amp. Using an electret-microphone sensor, the circuit activates a buzzer when the ambient sound exceeds a user-specified threshold. Resistor R_3 biases the microphone and capacitor C_1 blocks the microphone's DC signal component. IC_1 is connected as an inverting amplifier with adjustable gain. The amplifier cannot respond to positive inputs because the V^- terminal is grounded, and without sound the amplifier's input and output are near 0V. The output drives an RS (reset-set) flip-flop formed by the cross-coupled CMOS Nor gates. Therefore, in the absence of sound the flip-flop's Q output is high, and the buzzer is off. IC_2 's negligible standby current and the low quiescent current of the microphone and op amp ensure long battery life.

Sound detector has adjustable threshold

Sound causes the microphone to produce an AC signal whose reference is ground on the other side of C_1 . (The capacitor you choose should have low leakage current). This signal's negative excursions produce positive excursions at the flip-flop's S input. If the amplifier's gain (set by R_1) is sufficient, the signal at S will cross the gate's switching threshold and latch the /Q output low, activating the buzzer. The buzzer will remain on until you reset the latch by momentarily pressing S_1 . Remember that high closed-loop gain settings will reduce the

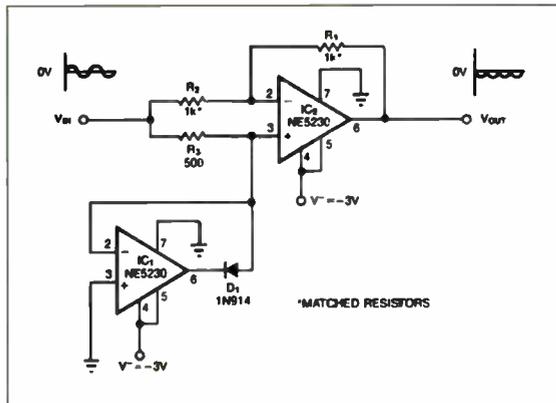


Fig. 4. This circuit (obtained by reversing the power supply connections in Fig. 3) performs negative full-wave rectification using a single supply voltage.

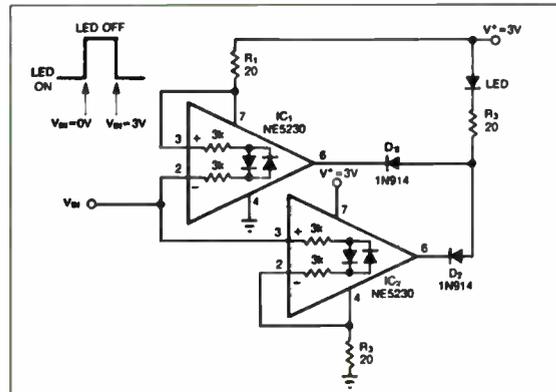


Fig. 5. This window detector's rail-to-rail input range allows the circuit to detect faults in which the input signal becomes shorted to either rail.

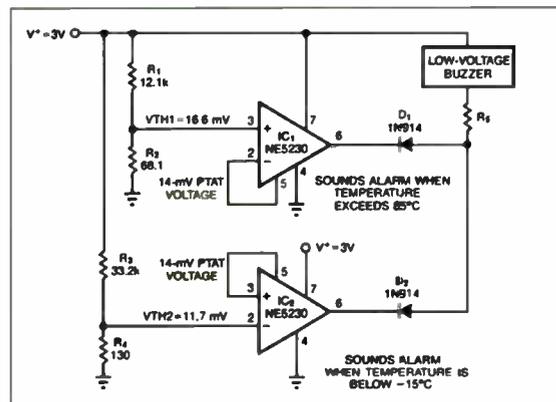


Fig. 6. The op amp's bias-adjust pin (pin 5) is the PTAT (proportional to absolute temperature) voltage, which lets you use the amplifier as a temperature sensor. This circuit activates the buzzer when the temperature exceeds a user-specified limit.

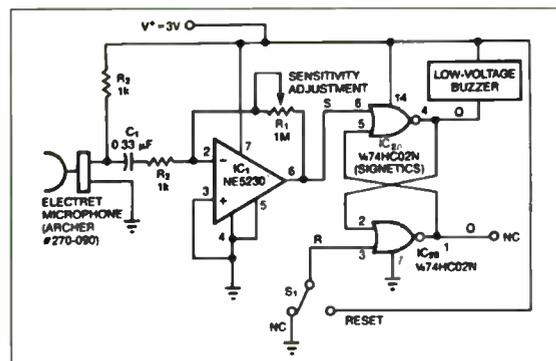
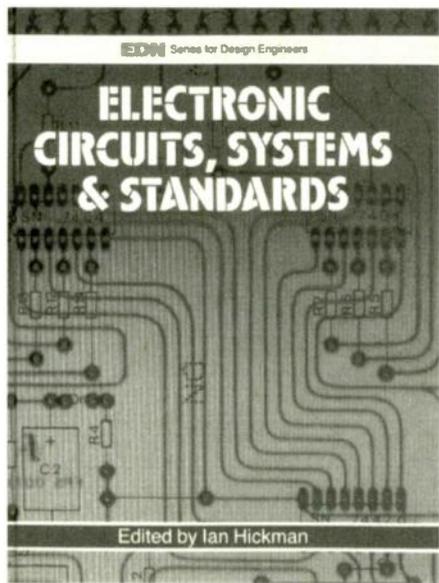


Fig. 7. Ambient sound above a user-determined threshold activates this intrusion detector. Once triggered, the alarm will sound until you momentarily press the switch (S_1).

circuit's sensitivity to high-pitched sound by lowering the amplifier's -3dB bandwidth. If you need more sensitivity, you can cascade two op amps and split the required gain between them.

Circuits that process ground-referenced signals often require dual power supplies, but dual-voltage battery supplies can increase a system's size and cost. You can avoid this extra hardware in some cases by converting a single 3V lithium-battery output into a ± 1.5 V output (Fig.



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8a). The R_1/R_2 divider splits the 3V supply, and the op amp's 40nA input-bias current offers a minimal load to the divider. The amplifier's output becomes the common terminal for all ground-referenced loads and signals.

The NE5230's low output impedance minimises any offset voltage created by the connection of loads between

the amplifier's output and V^- or V^+ . Moreover, the dual voltages track in magnitude as the battery cell discharges – a feature useful in applications that must maintain a precise voltage null despite fluctuations in the supply voltages. Figure 8a circuit sources and sinks 15 and 24mA, respectively.

To obtain higher load currents, you can connect two NE5230s in parallel (Fig. 8b). The difference in offset voltages (ΔV_{OS}) appears across R_3 and R_4 . The standby current in one op amp increases by $\Delta V_{OS}(R_3+R_4)$ but current in the other op amp decreases by the same amount, so the sum of the supply current through the two op amps remains constant.

Large load currents divide equally between the two op amps, and you would expect this circuit to provide twice the output current of Fig. 8a, but the load-current capability is generally less because of mismatch in the op amp's output resistances and mismatch between R_3 and R_4 . The Fig. 8b circuit sources and sinks 24 and 35mA, respectively, when operating from a 3V supply.

Bridge transducers for precision applications usually require an accurate low-drift voltage reference and a precision instrumentation amplifier (see box "What you

Fig. 8. The circuit in (a) converts a 3V cell into a $\pm 1.5V$ dual tracking supply. By connecting two amplifiers in parallel (b), you can nearly double the circuit's load-carrying capability.

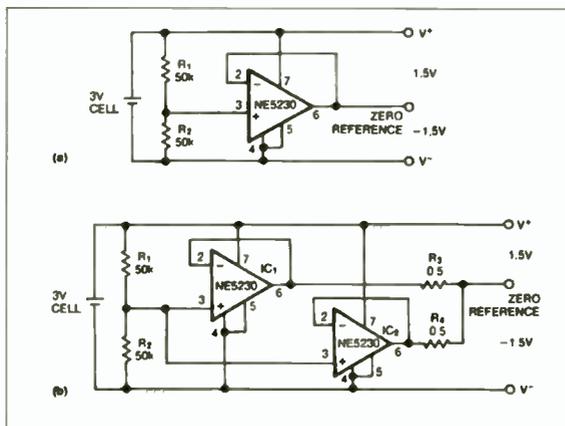
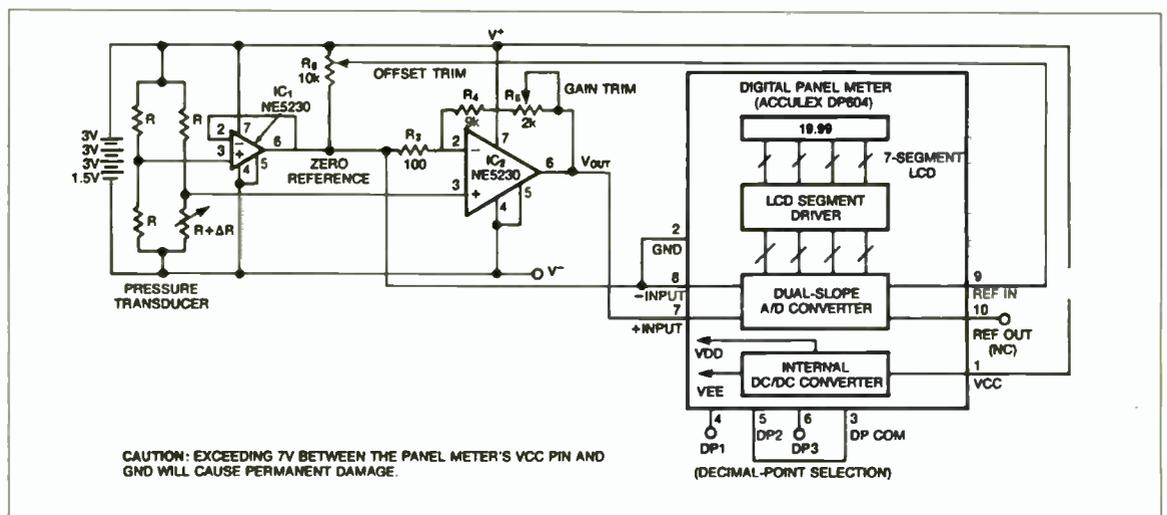


Fig. 9. This bridge transducer interface circuit conditions the bridge's output signal for ratiometric operation and eliminates the need for a reference voltage and an instrumentation amplifier.



CAUTION: EXCEEDING 7V BETWEEN THE PANEL METER'S VCC PIN AND GND WILL CAUSE PERMANENT DAMAGE.

(DECIMAL-POINT SELECTION)

should know about bridge circuits"). The Fig. 9 circuit, however, acquires and displays the bridge transducer's output without using a voltage reference or an instrumentation amplifier.

Op amp IC_1 buffers the fixed arm of the bridge and provides a reference potential for all ground-referred loads. Choosing this node as the reference potential converts the bridge's differential output signal to a single-ended signal referred to ground. This reference remains halfway between V^+ and V^- even if the battery discharges. The reference potential is thus a floating ground, often called an active guard.

Converting the bridge's differential signal to a ground-referred signal eliminates the bridge output's common-mode voltage, which also eliminates the need for common-mode rejection, usually obtained by adding an instrumentation amplifier. IC_2 amplifies the bridge's output signal, and R_5 lets you adjust the circuit's full scale output level.

The IC_2 output V_{OUT} will change as the batteries discharge, but the V_{OUT}/V^+ ratio will remain fixed. This relationship lets you remove the effect of battery discharge by operating the panel meter's A-to-D converter in the ratiometric mode. Connect the wiper of

R_6 to the converter's reference input to ensure that the signal and reference remain in proportion as the supply voltage changes. Finally, note that IC_2 amplifies its own input-offset voltage. You should null this effect by first balancing the bridge, and then adjusting R_6 for an all-zeros output at the panel meter.

Zahid Rahim, Signetics Corp

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What you should know about bridge circuits

A bridge circuit, often known as a Wheatstone bridge, consists of a pair of series-connected resistors connected in parallel with a similar pair of resistors (Fig. A). Bridge circuits are widely found in precision-null applications because the differential voltage ($V_1 - V_2$) across the bridge is 0V when the bridge is balanced.

What's more, this balanced condition is unaffected by voltage drops across line resistances or shifts in the reference voltage V_R . You can use such a balanced bridge to measure capacitance, inductance, or its own frequency of excitation (when applied in place of V_R).

A more common application for a bridge circuit is as a bridge transducer for converting physical parameters such as temperature or pressure into electrical signals. Normally, the resistance in one arm of the bridge varies with the measured parameter as resistances in the other three arms remain constant. This type of application usually includes a differential amplifier to amplify the bridge's differential output voltage.

The amplifier's output indicates any change in the measured parameter with respect to a reference level corresponding to the condition of a balanced bridge. You do need a fixed reference voltage; shifts in V_R will change the amplifier's output voltage unless the bridge happens to be balanced. The bridge's output

signal usually consists of several millivolts riding on a much larger common-mode signal.

Accordingly, you should choose a bridge amplifier that minimises inaccuracies through high common-mode rejection (CMR), low input-offset voltage (V_{OS}) and low V_{OS} drift with temperature. The amplifier should have high open loop gain to ensure a linear transfer function and low input-bias current to avoid loading the bridge. An instrumentation amplifier meets all these requirements and is designed specifically for conditioning the output of bridge transducers.

Note that even an ideal bridge amplifier will have a non-linear response because the bridge itself is inherently non-linear. The following derivation shows why:

$$\begin{aligned} V_0 &= A_{CL} (V_1 - V_2) \\ &= A_{CL} \left[\frac{V_R}{2} - \frac{V_R (R + \Delta R)}{R + R + \Delta R} \right] \\ &= -\frac{A_{CL} V_R}{4} \left(\frac{\Delta R / R}{1 + \Delta R / 2R} \right) \end{aligned}$$

A_{CL} is the amplifier's closed-loop gain. The bridge's output signal is non-linear because both the numerator and the denominator contain the transducer-deviation term ΔV . The signal is approximately linear over a small range of amplitudes, however. Such signals are held to low amplitude for that reason.

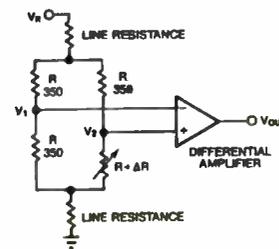


Fig. A. In a conventional transducer bridge, the parameter of interest causes a variation (ΔV) in the bridge's output. The amplifier senses the resulting small differential signal and also rejects the bridge's relatively large common-mode voltage.



MARCONI BEGINNINGS

Marconi in 1896 with some of his apparatus: the spark-generator on the left, and a Morse key to the right.

The first aerial (facing page, top left) was an elevated iron plate attached to the spark-gap. Another plate had to be buried in the ground, the lead for which can be seen tied to the left-hand table leg. This 1895 apparatus achieved a tenfold increase in transmission distance - from 100m to 1km

Progress leading up to Marconi's 1901 bridging of the Atlantic with wireless signals (*EW + WW*, December) had seen a development, in only eight years, from primitive table-top apparatus to the massive, high-powered (20kW equivalent input) installation at Poldhu.

Marconi's early experiments with radio transmission had begun in 1894, when he was 20. In 1895, while using slabs of sheet-iron to increase the transmitter spark's wavelength, he placed one on the ground, and held the other in the air. This, in effect the first aerial, produced a large increase in the signal strength, and in the range - from about 100m to 1km.

Marconi's transmitter consisted of a spark-gap between two metal spheres, attached to metal plates - one elevated, one buried in the ground.

The receiver used an identical aerial arrangement, attached to a coherer - an evacuated glass tube containing fine metal filings and closed by an electrode at each end. When a signal was received, the filings "cohered", their resistance dropped and a relay circuit was completed, enabling operation of a tapper and a Morse ink.

Marconi took out his first wireless patent in 1896. In September that year he conducted a demonstration on Salisbury Plain, for the benefit of the War Office and the

Post Office, at which a range of 1.75 miles was recorded.

Next year saw the bridging of the Bristol Channel, a distance of more than eight miles, and communication between the Royal Needles Hotel at Alum Bay on the Isle of Wight and a house in Bournemouth, which was almost twice as far.

In 1898, Lord Kelvin used the Alum Bay transmitter to send the first wireless-transmitted paid telegram. It read: "Tell Blyth this is transmitted commercially through ether from Alum Bay to Bournemouth and by postal telegraph thence to Glasgow".

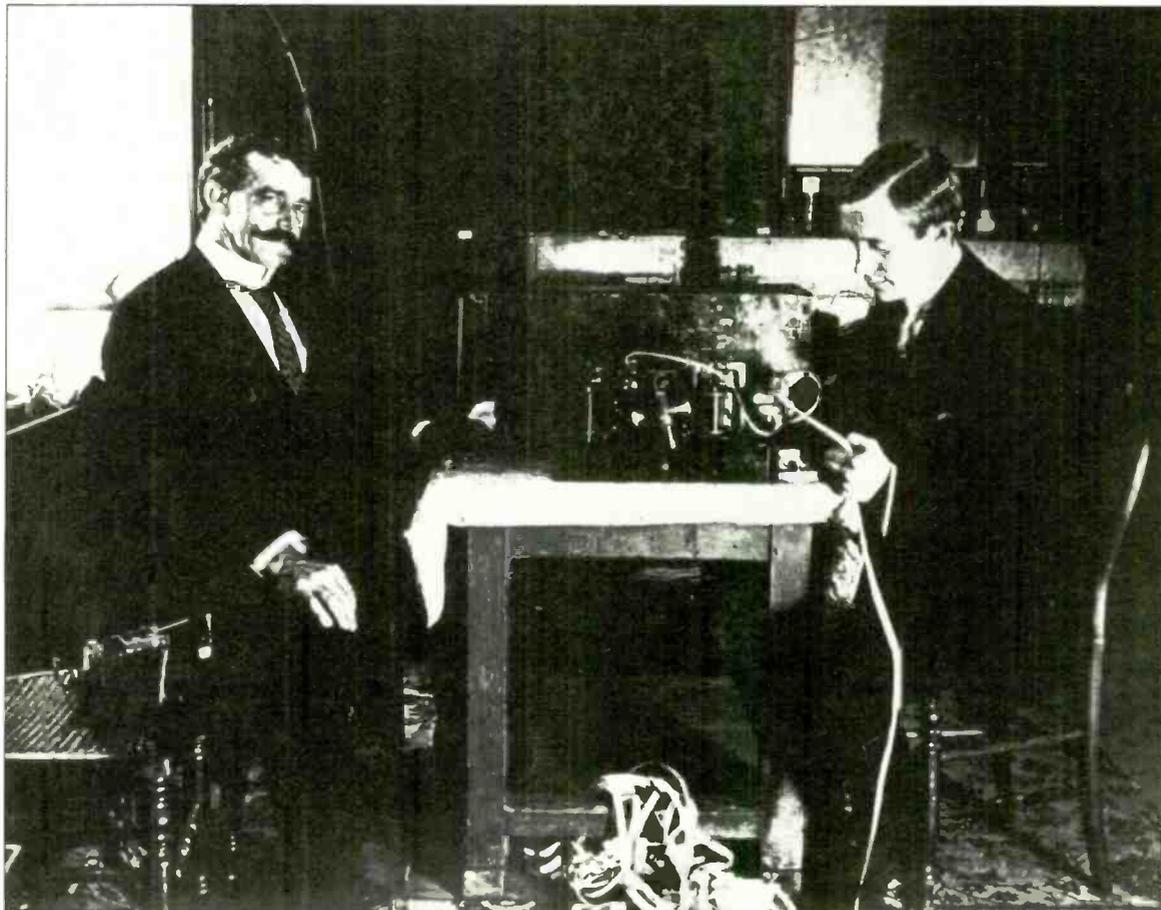
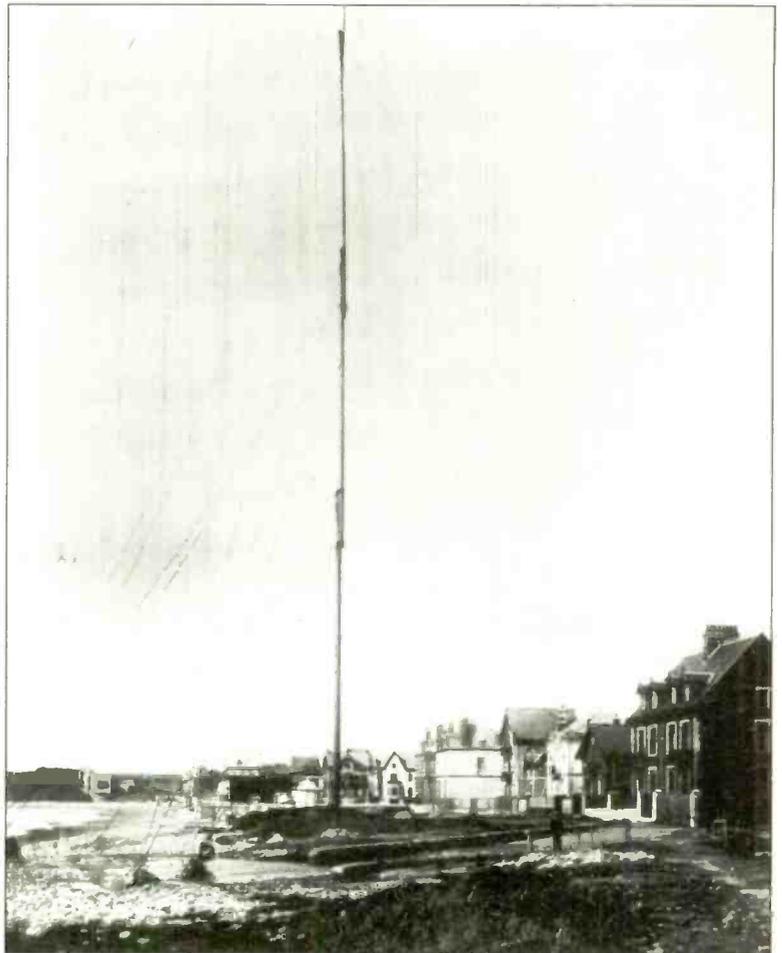
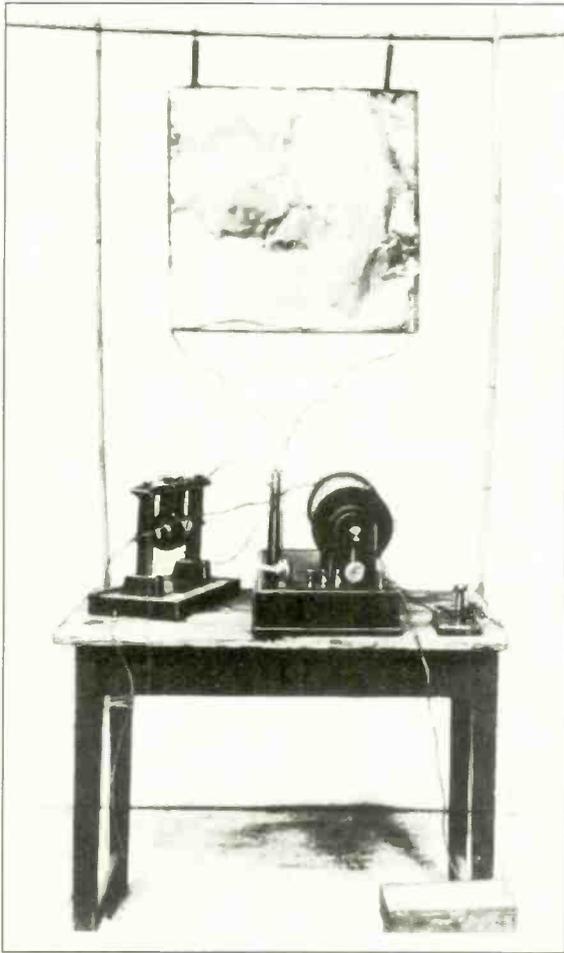
Kelvin's insistence on paying Marconi to send the message, and referring to it in the text, was intended as a challenge to the Post Office's monopoly on paid messages - a challenge it chose at the time to ignore.

Wireless distress

The Kelvin telegram was something of a stunt, but the first genuine use, as distinct from demonstration, of wireless telegraphy was not long in coming.

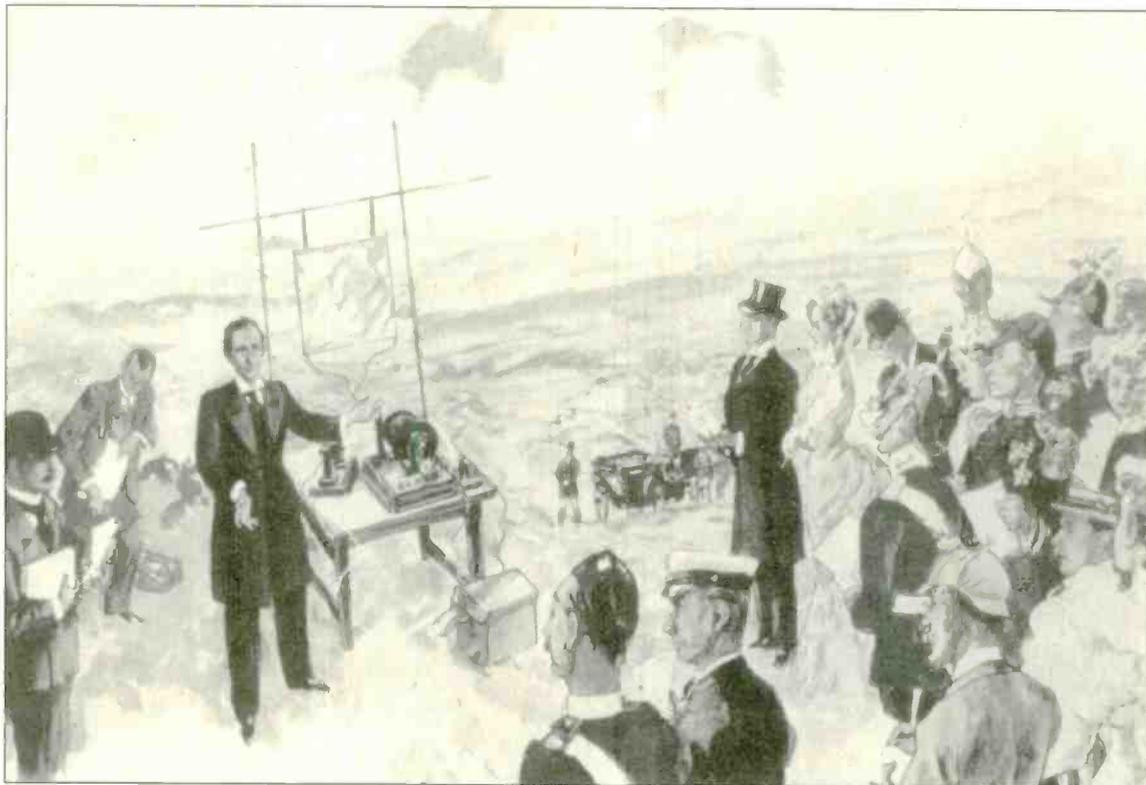
In 1899, the East Goodwin lightship, which had been rigged as a demonstration station, suffered storm damage and used its transmitter to send out distress signals.

Later the same year, it was struck by a ship and again used the transmitter, this time triggering the first sea



By 1899, signal range had increased sufficiently to cross the English Channel, between Wimereux, near Boulogne (above), and the South Foreland. The photo left shows a message being received at Wimereux. On the left is George Kemp, Marconi's personal assistant for over 30 years.

Marconi's 1886 Salisbury Plain demonstration, at which a range of 1.75 miles was recorded, was commemorated in a contemporary etching. It was probably drawn after the event since, although it identifies some of the War Office and Post Office officials present, it is not thought to be accurate in terms of the equipment used. Far larger aerials, probably suspended on balloons, would have been employed.



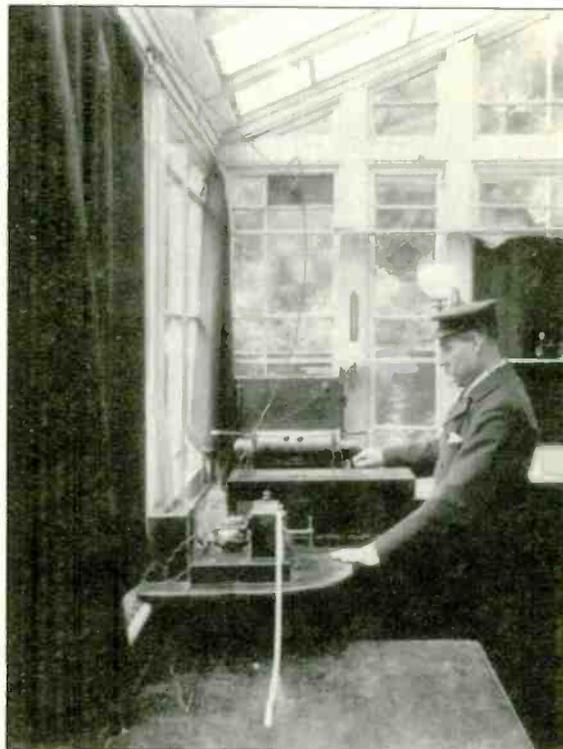
rescue in response to a wireless distress signal.

By 1899, transmission range had increased sufficiently to cross the English Channel, between Wimereux, near Boulogne, and the South Foreland. The signal proved strong enough to be picked up at Marconi's HQ in Chelmsford, 130km away.

By the turn of the century wireless was beginning to establish itself as a tool of communication, and in 1900 the Marconi International Marine Communication Company was set up.

Wireless was already being put to use in a variety of ways by 1900. Picture below shows the Mitcham Lane Fire Station, London, around 1900, with Station Inspector Preston despatching a message. The spark-generator near his right hand and the Morse printer in the foreground can both be clearly seen.

The East Goodwin lightship, rigged for demonstrations, sent the first wireless distress signals in 1899.



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CIRCLE NO. 136 ON REPLY CARD

Small loops are easy to tune but relatively insensitive. Large loops deliver more signal

IMPROVED HF RECEIVING LOOP

but at the expense of tuning range and omnidirectional lobe shape. Ronald Salter suggests that aerial loops based on parallel clover leaves overcome these limitations.

When selecting an aerial, the serious short wave listener is not well served since the repertoire consists of long wires, dipoles, whips, small tuned loops, and little else. More elaborate aerials don't always improve the signal to noise ratio. Rising interference levels, however, require new solutions.

At the writer's location, there is high voltage reticulation and an arterial road, while six nearby AM broadcast transmitters produce cross-modulation across most of the HF spectrum. Tests have shown that a small resonant aerial gives the best signal to noise ratio under these conditions. The aerial described here is three metres square and can be mounted on a pole or above a ceiling.

The noise reducing properties of small vertical loops are well known. Low radiation

resistance, and a figure-of-8 field pattern combine to give good signal/noise ratios. However, size limitations restricts sensitivity: a single-turn HF loop must be no more than 0.1λ in circumference, or the loop current becomes non-uniform and the field pattern breaks into lobes.

Typically, a 10MHz loop will have a diameter of less than 0.5m, and an area of about 0.2m². A 10MHz dipole has a conservatively estimated aperture area of 60m². Signal strength is, among other things, proportional to aperture area, so the difference is obvious. Loop gains reported in the literature are from -14dB, to -17dB w.r.t. a dipole. A loop larger than 0.1λ may also have too much inductance to be tuned with a practical value of capacitor, especially if it is shielded.

In addition, the need to tune and rotate the loop means that it must be near the operator, unless a remote control system is used. Much can be done however, to remedy the situation.

Firstly, mounting the loop horizontally gives an omnidirectional field pattern (Fig. 1). Low mounting height will raise the radiation angle, so the loop should ideally be at a height of $\lambda/2$, which is 25m at 6MHz; the prototype is giving good results at a height of about 6m.

Secondly, the aperture area can be enlarged while keeping the inductance low by putting multiple turns in parallel. These cannot be placed side by side as in a normal LF loop; doing so gives the effect of a single turn with a larger cross-sectional area and roughly the same inductance. However, if the turns are separated to minimize the magnetic coupling between them, the inductance looking into the network terminals (Fig. 2) is given by:

$$L_n = L_o/N \quad (1)$$

where L_n is the inductance of the network, L_o is the inductance of one loop, and N is the number of loops.

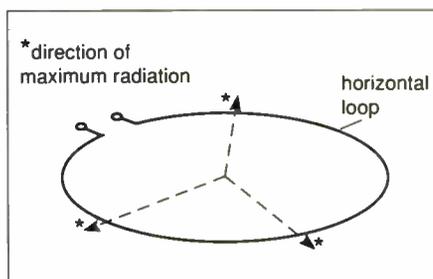
It follows from (1) that the individual loops in an N loop array can each be larger than a single loop having the same inductance as the array, and can cover the same frequency range using the same tuning capacitor. The prototype consists of four loops mounted horizontally in a clover leaf pattern.

Although the individual loop currents are non-uniform at $C/\lambda > 0.1$, the geometric symmetry of the array keeps the overall field pattern reasonably uniform.

Thirdly, varicap diodes at the aerial can provide remote tuning, balancing, and impedance matching; DC control voltages are conveyed by a multi-core cable strapped to the feed-line.

Fig. 3a shows a small loop with tuning capacitor C and load resistance R_L ; 3b the equivalent circuit. V_{oc} is the open-circuit induced signal voltage, $+j\omega L_o$ is the inductive reactance, R_r the radiation resistance, R_i the RF resistance, and $-j/\omega C$ the reactance of the capacitor. Let R_a be the total in-phase component of the loop impedance

Fig. 1. Radiation pattern from a simple loop.



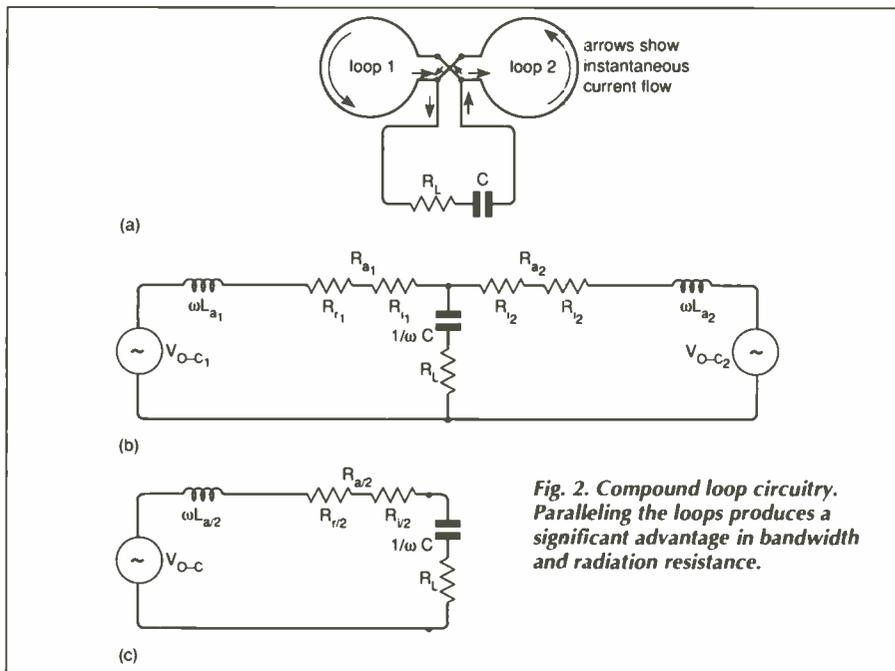


Fig. 2. Compound loop circuitry. Paralleling the loops produces a significant advantage in bandwidth and radiation resistance.

($R_a = R_r + R_i$). Then at resonance, $+j\omega L = -j\omega C$, and the voltage across R_L is given by:

$$V_{RL} = \frac{V_{oc} \times R_L}{R_a + R_L} \quad (2)$$

Figure 2a shows two identical loops mounted in the same plane, and connected so that their currents sum at the junction; 2b is the equivalent circuit. It can be shown that Fig. 3b can be replaced by the circuit of 2c. When $+j\omega L_a/2 = -j/\omega C$:

$$V_{RL} = \frac{V_{oc} \times R_L}{\frac{R_a}{2} + R_L} \quad (3)$$

It can be similarly shown that for N identical loops:

$$V_{RL} = \frac{V_{oc} \times R_L}{\frac{R_a}{N} + R_L} \quad (4)$$

$$\text{when } +j\omega L_a/N = -j/\omega C \quad (5)$$

We can now find the gain of an N loop array compared to a single loop having the same inductance. Maximum power transfer occurs when $R_L = R_a/N$: power developed in R_L is:

$$P_{RL} = \frac{V_{oc}^2}{4 \times \frac{R_a}{N}} \quad (6)$$

From (6) and appendix b, we can develop an expression:

$$10 \log \frac{C_2^4 \times R_{a1} \times N_2}{C_1^4 \times R_{a2} \times N_1} \quad (7)$$

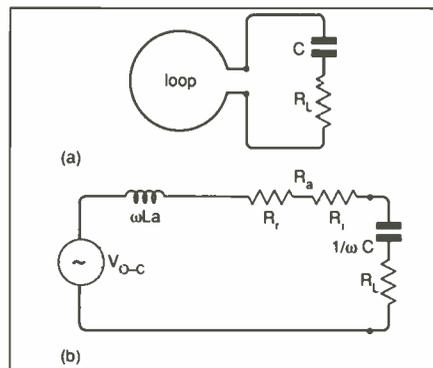


Fig. 3. Electrical circuit of a single tuned loop with resonating components.

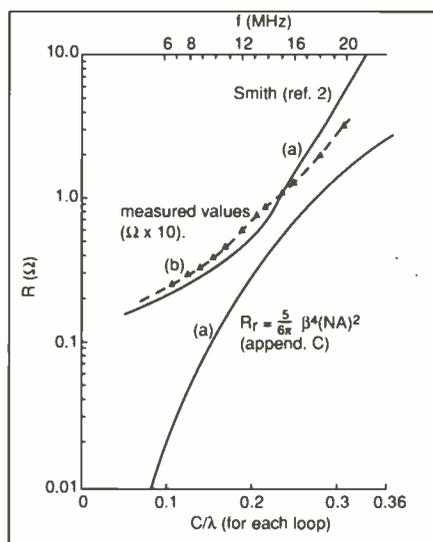


Fig. 5. Comparisons between expected and measured radiation resistance.

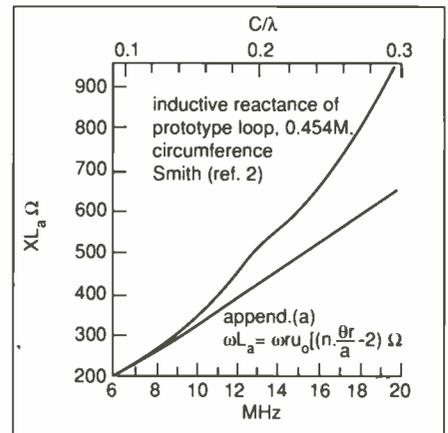


Fig. 4. Inductive reactance of prototype 0.454m loop

where C_l is the circumference of the single loop, C_2 is the circumference of one loop of the array, R_{a1} is the resistance of the single loop, R_{a2} is the resistance of the array, $N_1 = 1$ (for a single loop), and N_2 is the number of loops in the array.

There are no simple impedance relationships for larger loops; when $C/\lambda > 0.1$, both X_{La} and R_a rise faster than predicted (Fig. 4).

Masses of gain

Further, radiation coupling between close-spaced loops causes R_a to rise to much higher values than for one loop in free space. The writer measured R_a directly by two different methods; these were in substantial agreement (Fig. 5).

The prototype has four loops, each of 4.54m circumference, made from 5mm thick coaxial cable. At 10MHz the C/λ ratio = 0.15, $X_{La} = 87.5\Omega$ and $R_a = 3.6\Omega$. By extrapolation from the calculated performance of a 0.15m single loop aerial, the effective performance for the 4.54m four loop system is some 12dB better. This gives a gain of -2 dB to -5 dB w.r.t. a dipole - a good performance for a small antenna. Furthermore, this gain is available over 360°.

Equation 7 assumes circular loops, but no more than two such loops can be mounted side-by-side without overlapping. For $N > 2$, a shape other than a circle must be used; measurements on the prototype show this is not a major factor provided the departure from the circular form is not too great.

Realising this gain requires a match between the array R_a values, ranging from 2.4Ω at 6.5MHz, to 30Ω at 20MHz, and the load impedance - normally 50 to 70Ω. A shunt capacitor matching network was used in the prototype in conjunction with a balancing/matching transformer.

Inserting the R_a values in the appropriate

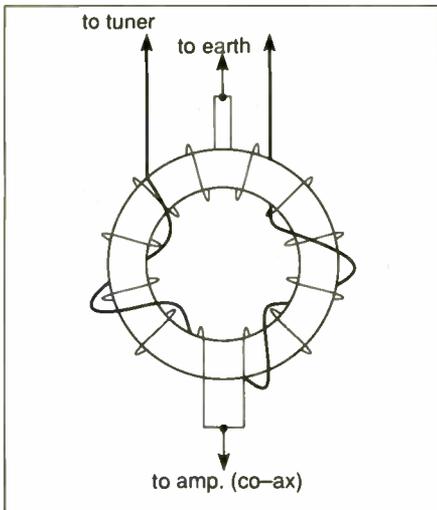
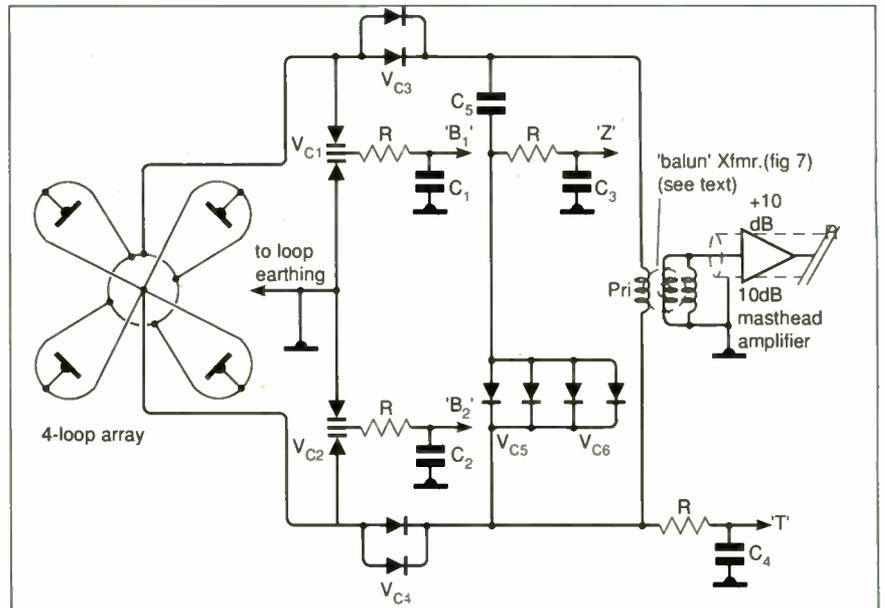


Fig. 6. Balancing/matching transformer.

equation gives a shunt capacitor vs frequency curve similar in shape to the tuning curve; the varicap voltages can then be arranged so that the shunt capacitance tracks the tuning capacitance across the frequency range and allows close to optimum matching. Although this is not of great importance in a receiving application, tests show it works quite well.

Constructional points

The transformer is wound on a toroid, and has two secondary windings of six turns each, wound in opposite directions, connected in parallel, and each spaced over half the core length. The four turn primary is wound over the secondaries and occupies the full core length (Fig. 6). This arrangement attempts to balance inter-winding capacitance while retaining full core usage. Tests with a source and load show high transmiss-



sion efficiency and an essentially flat frequency response (1dB).

RF balancing is by varicaps to earth from each side of the array. Their control voltages mimic the action of a differential capacitor - as one voltage rises, the other falls. Thus the effect of the balancing circuit on the tuning calibration is minimised, while still allowing a large change in the balance point.

The prototype array is shown in Fig. 7. Needing to suspend it between masts, the writer produced an assembly of spars, spreaders, wire and rope worthy of the Wright brothers. Each loop is earthed at its mid-point to minimise broadcast crossmodulation; the earth conductors are two metal

spars, and two lengths of coax strapped to the support rope. All four join at the centre.

Loop phasing is important. Each loop exits, curves clockwise (looking from above) and enters below. The four starts are joined inside a top cap; the four ends are joined in the tee body. Flexible leads and screw connectors connect these joins to the tuner.

Figures 8(a) and 8(b) show the masthead tuner and control circuitry. The emitter follower allows the tuning, matching, and balance voltages to follow the setting of the tuning potentiometer. It has been found convenient to allow the balancing voltage to follow the tuning also; this allows roughly constant adjustment of the balance pot at different frequencies. Occasionally, a better s/n ratio is obtained by reducing the balance voltage below the maximum, but this happens so rarely that the balance voltage pot may be eliminated if desired, the supply for the balance network being taken direct from the emitter of the transistor.

The tuner exhibits an apparent double-humped tuning characteristic, due to the array coming to balance at resonance. To tune, set the balance pot central, adjust tuning to mid way between noise peaks, then reset balance pot. If a noise null cannot be found (a rare occurrence) slight adjustment of the Z-match will often help. While the exact reason for this latter phenomenon is not apparent, it may be that adjusting V changes the phase relationship between the signal current and components flowing in the array earth network.

The modest gain (+10dB) line amplifier was an after thought, and is useful particularly at the lower frequencies. At the top of the spectrum, a little white noise is apparent, which may be reduced by lowering the amplifier supply voltage to about half the normal value.

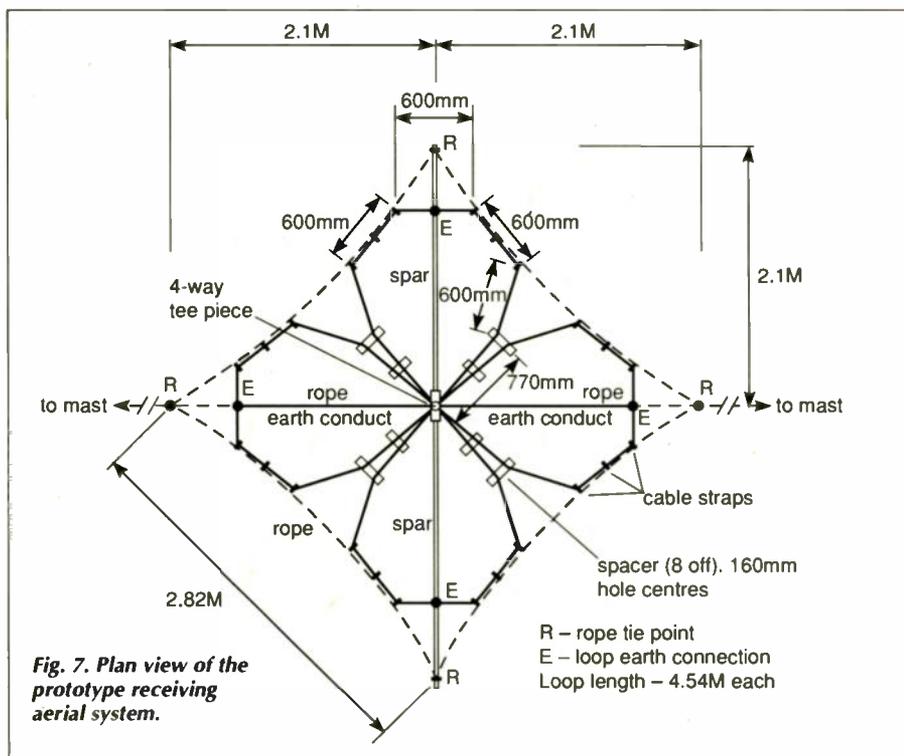


Fig. 7. Plan view of the prototype receiving aerial system.

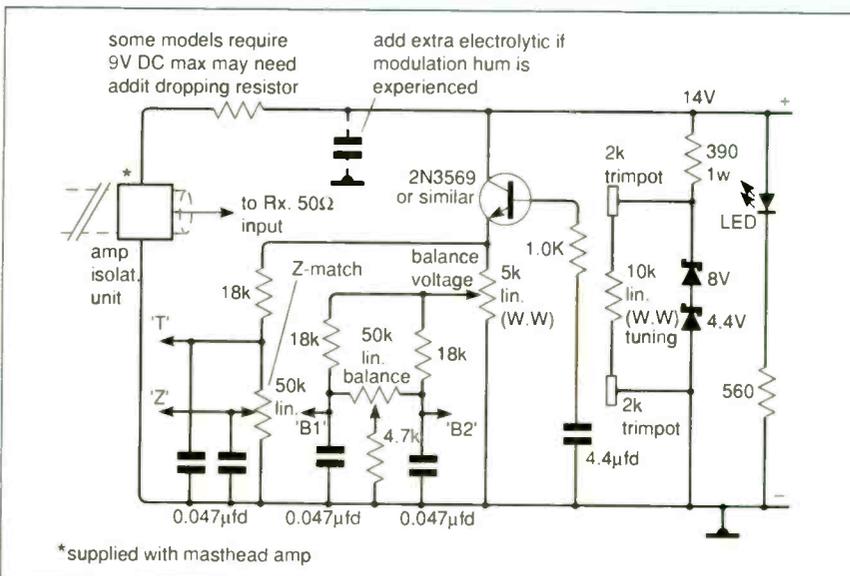


Fig. 8. Tuning and control circuitry. 8(a) (left) masthead tuner; 8(b) above) control box.

Performance

The writer has compared the loop array performance, over several years, against three other aerials: a 2m long tuned whip, a 35m wire, and an array of three dipoles cut logarithmic fashion across the frequency range. Accurate measurements are difficult – but an idea of performance has been gained.

The calculated figure of +12dB w.r.t. a

loop, and –3dB w.r.t. a dipole, at 10MHz, has been confirmed. No attempt has been made to measure the field pattern, but where the dipoles and long wire are clearly directional, no such property has been observed.

As expected, broadcast cross-modulation is severe with both the long wire and dipoles, but is scarcely observable with both the whip and the loop array.

Table 1. Summary w.r.t the dipole set.

Frequency	Long wire	Loop array	Whip
7MHz	–2dB	+3dB	–3dB
11MHz	–3dB	+8dB	0dB
17MHz	–0.5dB	+10dB	–1dB

The most important property, the signal/noise ratio, depends on the frequency and the conditions – i.e. the current level of electro-magnetic noise.

Table 1 gives a summary at three frequencies w.r.t the dipole set. These figures, based mainly on receiver AGC measurements, do not accurately reflect the ability of the loops to reject impulse noise, especially at the lower frequencies. Tape recordings have been made of signals which are clear and legible on the loop array, but unreadable on all other aerials. The performance of the loops is such that the whip and dipoles have been discarded, the long wire being retained only for demonstration purposes. ■

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Looking into a crystal memory

Massive but miniaturised storage capacity has been the computer industry's ultimate goal for over a decade. When magnetic bubble memories came about in the late 1970s they were highly regarded as a major leap forward. But now, following from observations made by a team of physicists during the course of a research project, there may be a new way of developing high capacity storage systems.

The research project is taking place at Oxford University's Physics Department (the Clarendon Laboratory), and the aim is to study the magnetic properties of crystals containing rare earth ions.

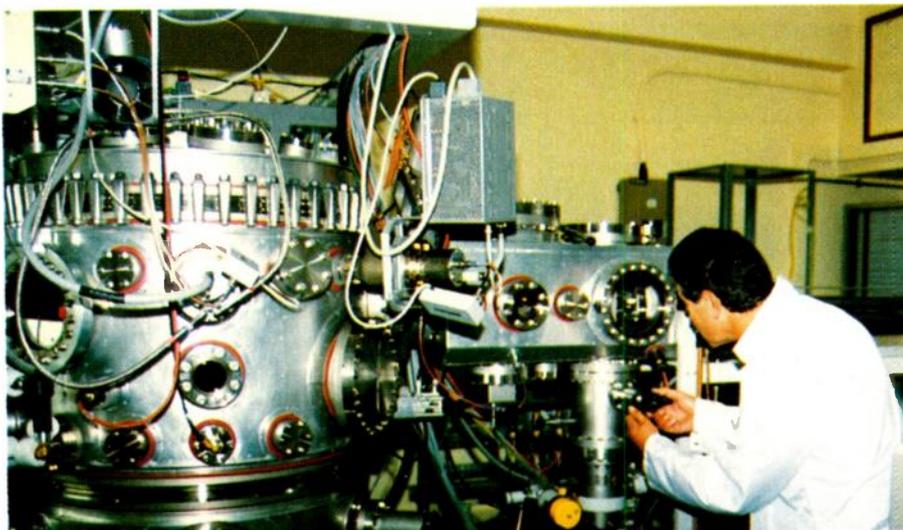
As part of the project the team is developing rare earth multilayers and superlattice structures by using an ultra high vacuum deposition plant.

Layers of magnetic and non-magnetic atoms are deposited in succession to form a multiple sandwich repeated about 100 times in coherent epitaxy. The atomic layers are deposited in a regular coherent array – more akin to materials engineering, putting rafts of atoms on top of each other. The layers, each of which can be about two atomic

Results from a project at the Clarendon Laboratory shows the production of memory systems made out of stacks of atoms may at last be possible. Shaz Horner reports.

buffer layer. The substrate/buffer system provides the atomically smooth and regular surface on which the rare earths can be deposited in any desired sequence or thickness, and built up atomic layer by atomic layer.

It is when the designed crystal structures are placed in a magnetic field that they show "interesting properties". According to the team: "New and unexpected magnetic phenomena have been observed in these designer materials which suggest tantalising possibilities for device application". One example is that in a multilayer



Looking for "New and unexpected magnetic phenomena": Mike Wells of the Oxford team examines the loaded cassettes in the UMS 630 at the Clarendon Laboratory

layers thick, are deposited by using molecular beam epitaxy (MBE) - this is where the project gets its name; LaMBE. La comes from the lanthanide series of rare earths. MBE has been in use for sometime for semiconductor deposition and for the development of high temperature superconductors.

The resulting sandwich is thin at about 50 Angstrom or less.

Alternating layers are deposited on a sapphire substrate coated with a niobium

structure where the "particular" rare earth metals and the thicknesses of the layers are optimised, "metastable magnetic states" are observed.

In these states the magnetisation vector for neighbouring rare earth ions along a specified direction, form a left handed or right handed helix depending on magnetic and thermal history. In addition the magnetic behaviour is translated through the layers - one layer talks to another layer magnetically even if there is a non-magnetic

Deposition process

The laboratory uses a Serc funded Blazers UMS 630 customised to meet the project's specific requirements. The plant provides a vacuum of 10^{-11} mbar as well as computerised control of the evaporation process. Up to six substrates may be loaded onto a cassette system and are transferred one at a time, from the load-lock chamber into the main growth chamber. The growth chamber has been fitted with a specially developed cryogenic shield for protection against contamination during deposition. Currently the plant has two electron beam guns and one effusion cell but there is capacity for expansion. These provide the sources of rare earth metal vapour and niobium.

According to the LaMBE team a particular advantage of the plant is the provision of a quadrupole mass spectrometer to monitor the evaporant beams from the electron-gun-heated hearths. The measured flux is compared with a reference value and the difference is fed back to the electron gun controller. Slow control in the range of seconds is affected by altering the filament current of the electron source. Fast control in the range of ten milliseconds is produced by changing the voltage on the Wehnelt shield surrounding the source of electrons thereby altering the number which arrive at the hearth.

layer in between. Therefore by assigning zero or one to each of the states respectively an n-digit binary number could be stored vertically through the n-layer sample.

If the results obtained from this research project can be harnessed for developing high density storage devices the consequences for the computer industry would be far reaching. The project could enable development of magnetic storage chips made of artificial crystals containing rare earth materials. It may prove to be the basis of devices with increased storage capacity and greater miniaturisation.

But one major hurdle still to be tackled would be finding a way to write and read data to and from such memories. A possible solution could be the use of variable intensity, focused laser radiation which uses the skin-depth effect, according to the LaMBE team

Nonetheless, the project's aim at present is to grow and understand the physical properties of the crystals. Finding a way to read or write the information, would be a problem for engineers to solve.

As to why rare earth metals are used for the research project, the team say that rare earth ions have smaller inter-atomic interactions which make them more "amenable" to investigations. The magnetic behaviour of a rare earth ion arises from its incomplete shell of electrons. This shell is shielded by conduction electrons and therefore the effects observed are easier to piece together than would be the case with transition metals such as iron and cobalt.

Shaz Horner

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REGULARS

RF CONNECTIONS

Low-cost synchronous detection

Direct-conversion receivers have a number of fundamental advantages over competitive techniques. But up to now nobody has yet marketed a direct-conversion receiver with synchronous demodulation for broadcast signals at a competitive price. However a recent patent application for design of a synchronised double-sideband AM broadcast receiver with no IF stages could change all that.

One of the important advantages of direct-conversion receivers is virtual elimination of spurious responses, in particular image-response. Benefits also include the opportunity to utilise the linear demodulated signal for effective post-detector filtering (including digital signal processing). This is preferable to IF filtering based on crystal filters of limited dynamic range which exhibit non-reciprocal characteristics.

Considerable use has been made of direct conversion, particularly for simple low-cost SSB/CW receivers built by amateurs without fully synchronous I, Q demodulators. But the technique is suitable for simple applications such as paging receivers where it is possible to integrate the entire receiver on a chip. Direct conversion is also seen as one way of implementing digital HF receivers, although in this case there is usually a preliminary mixer and broadband IF.

Over the years there have been a few designs for synchronous detection receivers for the reception of MF/HF AM broadcast stations, but only those based on superhet-type front-ends seem to have reached the market-place.

Some years ago Phase Track of Reading introduced a portable superhet receiver, crystallised for a limited number of HF broadcast channels (eg BBC World Service) that featured synchronous AM detection to counter distortion due to selective fading. Later, for general coverage, a model with a frequency synthesizer was marketed.

More recently, Sony has marketed an "enthusiast's receiver" with synchronous detection and provision for reception of AM/SSB/NBFM/RTTY/FAX mode plus VHF/FM, including a massive bank of channel memories and also a built-in spectrum analyser to provide panoramic reception facilities for around £3000.

But, to the best of my knowledge, nobody has yet marketed a direct-conversion receiver with synchronous demodulation for broadcast signals at a competitive price.

Patent advance

This could soon change. In July, Edward Forster of Phase Track filed a patent application for design of a synchronised double-sideband AM broadcast receiver

Early developments

Almost 20 years ago, I wrote a two-part article for *Wireless World* on synchronous detection in radio reception (September and November, 1972) which drew attention to the attractions of the form of phase-locked-loop synchronous detector described by J P Costas of General Electric (US) as the basis of a high-performance direct-conversion HF communications receiver.

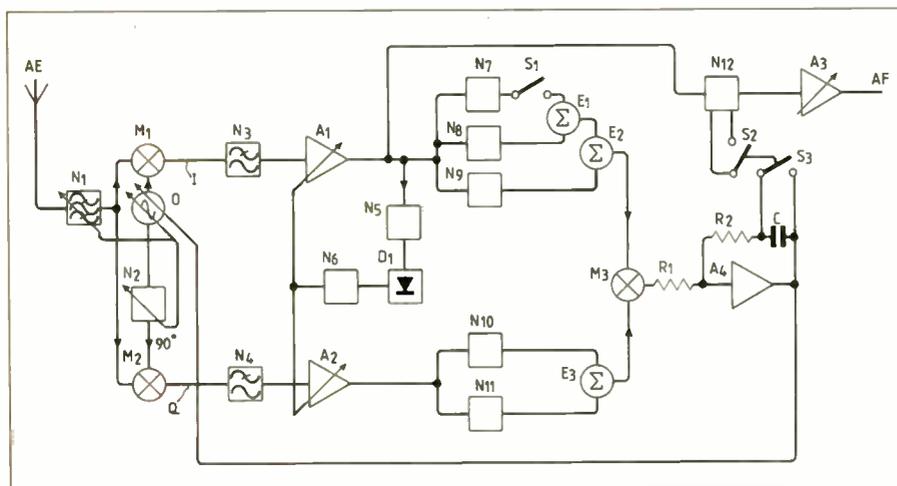
Costas was a powerful advocate of synchronous systems and direct-conversion (zero-IF) receivers in the 1950s. In the December 1956 issue of *Proc IRE*, an issue devoted almost entirely to advocacy of HF SSB with fully suppressed carriers, he struck an "odd-man-out" attitude in showing that the main arguments in favour of SSB were based on use of conventional envelope detection of AM, and would not apply if receivers fully utilised synchronous demodulation, permitting the use of double-sideband, suppressed-carrier transmissions as well as reception of conventional AM signals.

He outlined, as Professor DG Tucker had done previously, the practical advantages of direct-conversion rather than superhet principles and provided some detail of an experimental high-performance direct-conversion receiver with one of the then very complex frequency synthesizers – the AN/FRR-48 (XW-1) prototype with two-phase synchronous demodulation (using what has become known as the Costas loop), phase-locking the local oscillator by the use of an AM phase discriminator.

with no IF stages, aimed at low-cost receivers for the long, medium and short-wave bands (Fig. 1).

Elimination of the IF stages simplifies design of a receiver and should improve performance.

The receiver has no unwanted image responses and the bandwidth can be more accurately and cheaply set than with conventional IF filters. The only real spurious response, to the third harmonic, is easily filtered by a tracking pre-selector which may also usefully tune a small rod



EC Forster's direct-conversion synchronous receiver for AM or reduced-carrier SSB broadcast transmissions.

antenna giving better performance than untuned active antenna counterparts. Being synchronous, very little non-linear distortion is experienced compared with that found in conventional (AM) receivers using envelope detectors.

Forster believes that with direct-conversion, two-phase (I,Q) receivers, the key to making the synchronisation satisfactory is to ensure that it holds during modulation pauses. In his original (Phase Track) superhet design synchronisation is to the carrier alone, but since this is subject to severe fading on HF, characteristics of the loop had to be carefully adjusted so as to hold synchronisation during these fades and also maintain high spectral purity. The approach has now been applied to the direct-conversion receiver. However, there are many other interactions in such a receiver between the AGC, the high level carrier and the modulation which has to be adjusted for correct operation.

Initially it proved difficult to overcome such drawbacks. But now Edward Forster is convinced he has solved these problems. His aim is to develop a design that could make possible LW/MW/SW receivers at a cost comparable to the bottom-line superhet models with envelope detection now on the market. But these would be capable of outperforming superhet-type receivers, particularly on HF.

Looking for exploitation

Forster is currently trying to interest consumer-receiver manufacturers in his design. The demonstration prototype receiver uses a few standard IC devices but there is considerable scope to reduce the component-count with greater integration. The basic RF input sections are similar to those of superhet receivers but are simpler to implement since all sections track the same signal frequency.

The patent application acknowledges that the concept is based on the techniques described by Costas in 1956, by D Richman in "Colour carrier reference phase synchronisation accuracy in NTSC colour television". (*Proc IRE*, January 1954 and in British Patent GB 2 077 533). In the figure, *N1* to *N12* are passive networks (*N5* to *N11* simple resistor-capacitor networks); *A1* to *A4* are amplifiers; *M1* to *M3* mixers (preferably doubly-balanced mixers); *E1* to *E3* summing circuits.

In practice *N1*, *N2* and *O* are gang tuned, *N1* preferably being double-tuned with *N2* constructed using a low *Q* series inductor tuned by a shunt capacitor, one of the ganged sections.

Since no frequency-synthesizer is used, the spectral purity of the oscillator is very good and power consumption much lower than for synthesised receivers.

The patent application explains: "The output of amplifier *A4* frequency modulates oscillator *O* by a small amount which is nearly constant throughout the receiver's

Phasing-type SSB generation

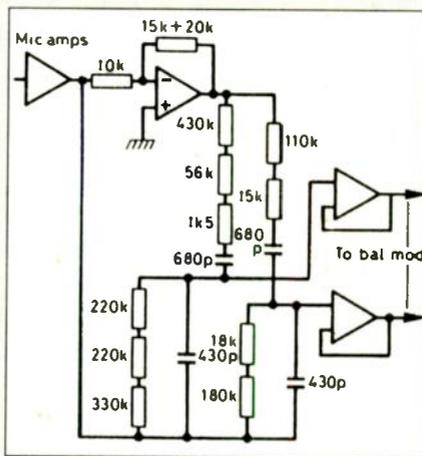
Much of early amateur-radio equipment in the then absence of effective SSB crystal and mechanical filters at HF, was based on phasing-type generators and occasionally phasing-type demodulators (with some later use of the Weaver "Third Method" and the Gingell "Polyphase" networks).

But in practice for many years virtually all commercially manufactured, and most home-built, SSB transceivers have used filter-type systems.

These are based on lattice-type HF crystal

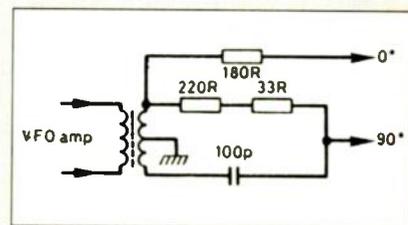
phasing networks and the difficulty in maintaining accurate phasing over an appreciable temperature range.

Recently, however, John R Hey, G3TDZ has been endeavouring to re-popularise classic phasing-type SSB generation as part of a "White Rose" club project designed to show that amateur SSB HF equipment need not involve factory-built £1000-plus transceivers. The White Rose project includes a 3.5MHz SSB exciter that takes advantage of the improved stability of modern components such



filter or crystal ladder filters, the latter type, where all crystals can be on the same frequency, can be based on low-cost colour-TV or "clock" crystals.

Phasing-type SSB generation tended to fall into disfavour largely because of the critical, non-standard component values required for 90° (±45°) wideband (300-4000Hz) audio



The RF phase-shift network (above) used for the White Rose constructional project. (*Radio Communication*, June 1991)

Practical realisation of the audio phase-shift network (left) using standard value components (1%) found to give excellent results between 150Hz and 4kHz. (*Radio Communication*, June 1991)

as metal film resistors, multi-turn cermet trimmers and polystyrene capacitors and use of combinations of standard 1% tolerance values to form audio and RF phase-shift networks that give excellent results between about 150Hz and 4kHz and between 3600 and 3800kHz (the SSB segment of the 3.5MHz amateur band).

frequency range so that loop gain remains substantially constant. This kind of feedback loop is known as a type II system where this refers to the number of integrators in the loop. The circuit *R1*, *C* and *A4* provide a virtually perfect integrator if adjusted correctly. Since the error output of *M3* is driven to zero by the loop action, momentary lapses of modulation can be accommodated since the loop control voltage is held by the voltage across *C*.

"Thus the circuit remains substantially synchronised at all times.

However, to help initial synchronisation and maintain synchronisation during path disturbances on short wave, some extra acquisition system is required. This is obtained by a frequency discriminator characteristic set about the carrier (zero baseband frequency) and operating below modulation frequencies so that it is not normally operative.

"This discriminator action is provided by the additional networks *N8* and *N10* which provide a high frequency gain and phase balance but a low frequency gain slope and phase unbalance. The gain of the

discriminator thus formed has to be adjusted to match the loop operation normally set for modulation control. As an aid to acquisition during tuning, network *N7* provides wider discriminator action operated by momentary switch *S1*.

"Summing circuits *E1*, *E2* and *E3* feed the resultant *I* and *Q* components to mixer *M3*. During tuning, it is desirable to short-circuit integrating capacitor *C* with switch *S3* and at the same time reduce the output volume by bringing into operation attenuator *N12* by closing switch *S2*. Finally the audio output *AF* is fed from the manually variable gain amplifier, *A3*."

The result appears to be an effective and simple-to-operate receiver of improved performance.

Whether Edward Forster will be able to convince the traditionally-conservative consumer industry to market receivers based on his patent-application remains to be seen; one can hope only that somebody will be prepared to give this promising development a whirl.

Pat Hawker

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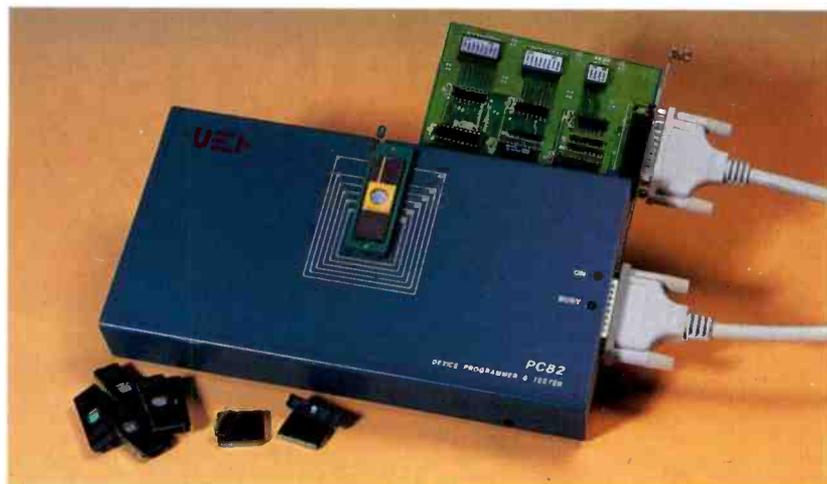
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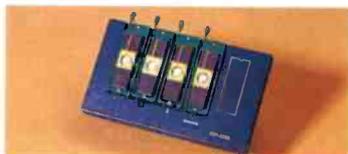
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